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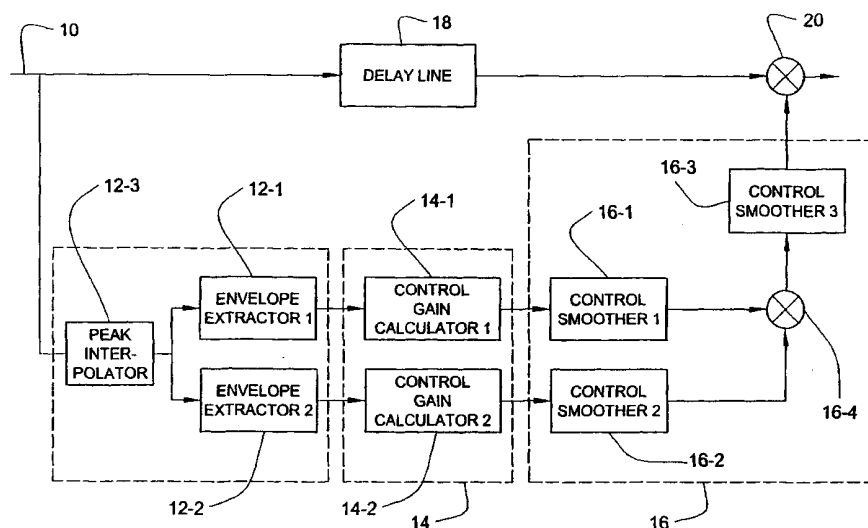
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- (71) Applicant (for all designated States except US): K. S. WAVES LTD. [IL/IL]; Azrieli Center, Round Tower, 21st Floor, 132 Derech Petach-Tikva, 67021 Tel Aviv (IL).
- (72) Inventor; and
- (75) Inventor/Applicant (for US only): SHASHOUA, Meir [IL/IL]; 32 Fireberg Street, 63827 Tel Aviv (IL).
- (74) Agent: REINHOLD COHN AND PARTNERS; P.O. Box 4060, 61040 Tel-Aviv (IL).
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(54) Title: DYNAMIC RANGE COMPRESSOR-LIMITER AND LOW-LEVEL-EXPANDER WITH LOOK-AHEAD FOR MAXIMIZING AND STABILIZING VOICE LEVEL IN TELECOMMUNICATION APPLICATIONS



(57) Abstract: A voice signal processing system with multiple parallel control paths, each of which address different problems, such as the high peak-to-RMS signal ratios characteristic of speech, wide variations in RMS speech levels, and high background noise levels. Different families of input-output control curves are used simultaneously to achieve efficient peak limiting and dynamic range compression as well as low-level dynamic expansion to prevent excessive amplification of background noise. In addition, a delay in the audio path relative to the control path makes it possible to employ an effective look-ahead in the control path, with FIR filtering smoothing-matched to the look-ahead. Digital domain peak interpolators are used for estimating the peaks of the input signal in the continuous time domain.

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**DYNAMIC RANGE COMPRESSOR-LIMITER AND
LOW-LEVEL-EXPANDER WITH LOOK-AHEAD FOR
MAXIMIZING AND STABILIZING VOICE LEVEL IN
TELECOMMUNICATION APPLICATIONS**

FIELD OF THE INVENTION

The present invention relates to voice processing and, more particularly, to voice processing for telecommunication and other narrow dynamic range voice communication systems, where it is desired to maximize and stabilize the level of
5 received or transmitted speech.

BACKGROUND OF THE INVENTION

Speech signals are characterized by a large dynamic range and high peak-to-RMS ratio. In telephone applications, especially cellular telephone, this dynamic range is further exaggerated due to variations in relative positioning of the talker
10 and microphone, variations of voice level between different talkers, variations in same talker's voice level, and similar variable factors.

On the other hand, the reproduction circuitry of common telephones are limited in their dynamic range, especially for cellular phones where supply voltage, physical size, and cost are a further limiting factor. An extreme example is the
15 cellular/mobile speakerphone, where despite severe restrictions on the dynamic range, satisfactory listening requires a minimum loudness level from the speakerphone.

There are three major problems associated with dynamic range in telephone applications:

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- the high peak-to-RMS ratio naturally characteristic of speech signals;
- the wide variations in RMS level of speech signals; and
- the high level of background noise typically encountered in telephony applications.

5 Treating the speech signal by applying signal processing techniques can significantly improve the situation, but as will be explained, each of the above problems requires a different treatment in order to achieve optimal results.

Various methods and circuits are known in the prior art for automatic gain control (AGC), such as disclosed in US Patent 5,854,845 to Itani, US Patent
10 5,832,444 to Schmidt, and US Patent 5,838,194 to Khoury.

None of the prior art methods, however, fully address all of the above-mentioned problems, but provide for only limited improvements. While such limited improvements may have been sufficient for traditional telephony, they are not adequate to deal with the more severe problems posed by
15 cellular/mobile telephony.

The automatic gain control methods described in the prior art incorporate an input-output target response that allows no dynamic variation in the signal range (the target output level is constant except when noise is detected). This is a highly unnatural output target response, which forces using a slow response time
20 in order to permit some reasonable dynamics of the processed speech signal. Another factor that slows down the response is the need to decrease the amount of audible distortion introduced into the signal.

On the other hand, controlling signal peaks demands a short response time, and therefore controlling signal peaks is not possible when a slow response time
25 is used. For this reason, prior art methods fail to reduce the high peak-to-RMS ratio of speech, and sometimes even increase it, as can be seen for example in Khoury (US Patent 5,838,194), figures 13 and 14.

On the other hand, controlling signal peaks demands a short response time, and therefore controlling signal peaks is not possible when a slow response time
30 is used. For this reason, prior art methods fail to reduce the high peak-to-RMS

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ratio of speech, and sometimes even increase it, as can be seen for example in Khoury (US Patent 5,838,194), figures 13 and 14.

Another limitation of prior art methods is that they deal with both the AGC of the speech signal, as well as with the muting or reduction of background noise traveling through the same signal path. This forces a single method of
5 detecting the envelope; the response times involved, and the smoothing applied, to deal with significantly different problems. Because of this, the performance of such methods is degraded.

There is thus a widely recognized need for, and it would be highly
10 advantageous to have, a means of that can simultaneously of automatically maximizing and stabilizing speech signals that can handle a high peak-to-RMS ratio, wide variations in RMS level, and high levels of background noise. This goal is met by the present invention.

SUMMARY OF THE INVENTION

15 It is an object of the present invention to provide a method for processing speech signals that provides an optimal solution for all the previously-mentioned problems, and allows for maximizing and stabilizing the RMS voice level, significantly reducing the peak-to-RMS ratio, and avoiding excessive amplification of background noise.

20 The present invention discloses several novel concepts that significantly alleviate the above mentioned problems. These novel concepts are:

1. Implementing more than one control path in a parallel fashion, where each path addresses a different problem. This permits a separate optimizing of the envelope estimation method and response time,
25 control curves, and the control signal smoothing method and response time.
2. Utilizing a family of input-output control curves suitable for both peak limiting and dynamic range compression (herein denoted as compressor-limiter control curves).

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3. Utilizing a family of input-output control curves suitable for preventing excessive amplification of background noise. (herein denoted as low-level expander control curves).
4. Delaying the audio path to allow for look-ahead in the control path.
- 5 5. Utilizing finite input response (FIR) filtering smoothing matched to the look-ahead.
6. Utilizing digital domain peak-interpolators for estimating the peaks of the corresponding input signal in the continuous time domain.

Figure 1 shows a generic block diagram according to the invention and
 10 illustrates the use of multiple parallel control paths. Signal paths **22** and **24** carry at least one signal and implement the parallel control path principle of the present invention. An input signal **10** is fed in parallel into a delay line **18** and an envelope extractor **12**. Envelope extractor **12** extracts at least one envelope of input signal **10**. More than one envelope will be extracted for a multiple parallel
 15 control path. The envelopes are fed via signal path **22** to a control gain calculator **14**. Control gain calculator **14**, calculates a gain for each envelope, and the gains are fed via signal path **24** to a control smoother **16**, which smoothes the gains and delivers a single consolidated output control gain, which is in turn applied to the output of the delay line at an output multiplier **20** to produce the
 20 final output.

According to the present invention there is provided a voice signal processing system receiving an input signal characterized by at least one envelope, the system having an output signal and a specified maximum gain, the system including: (a) an input for receiving the input signal; (b) an envelope extractor
 25 coupled to the input for extracting at least one envelope of the input signal; (c) a control gain calculator coupled to the envelope extractor, for calculating at least one gain, wherein the control gain calculator is operative to performing a calculation of

the group containing: (i) a first gain calculation of $\frac{1}{1/Gain + (1 - 1/Gain) * Env}$,

wherein *Env* is an envelope and *Gain* is the specified maximum gain; (ii) a second

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gain calculation of the minimum of 1.0 and Env/Th , wherein Th is a threshold below which the result of the second gain calculation decreases; and (iii) the product of the first gain calculation and the second gain calculation; (d) a control smoother coupled to the control gain calculator for smoothing the at least one gain, 5 and for delivering as the output signal a control gain; (e) a delay line coupled to the input, to produce a delayed input; and (f) an output multiplier coupled to the delay line and to the control smoother for applying the control gain to the delayed input.

BRIEF DESCRIPTION OF THE DRAWINGS

The invention is herein described, by way of example only, with reference to 10 the accompanying drawings, which:

Fig. 1 shows a generic block diagram according to the present invention.

Fig. 2 shows an embodiment of the invention using two parallel control paths.

Fig. 3 is a graph of the compressor-limiter control gain versus envelope 15 according to the present invention.

Fig. 4 is a graph of the low-level expander control gain versus envelope according to the present invention.

Fig. 5 shows the effect of look-ahead, and look-ahead in combination with recursive or FIR filter smoothing, according to the present invention.

20 **Fig. 6** shows the effect of continuous domain peak estimation according to the present invention.

Fig. 7 shows a block diagram of a peak estimator using all-pass filters according to the present invention.

Fig. 8 shows an embodiment of the present invention where N audio 25 channels are processed together.

Fig. 9 shows an embodiment of the present invention where N audio channels are processed together, and where each channel has a dedicated peak interpolator.

Fig. 10 shows an embodiment of the present invention where two audio

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channels are processed together, and where each channel has a dedicated peak interpolator.

Fig. 11 shows an embodiment of the present invention where signal processing is applied to the sum of several individual signals in a video conferencing or teleconferencing application.

Fig. 12 Shows an embodiment of the present invention where the envelope detector is omitted from one of the control signal paths.

Fig. 13 shows an embodiment of the present invention where the envelope detector and the signal smoother are omitted from one of the control signal paths, and only smoothing by the final smoother is applied.

DESCRIPTION OF THE PREFERRED EMBODIMENTS

As previously noted, the three major problems associated with dynamic range in telephony applications are the high peak-to-RMS ratio natural to speech signals, the wide variations in RMS level of speech signals, and the high level of background noise typical to telephony applications.

The principles and operation of a compressor-limiter / low-level expander according to the present invention may be understood with reference to the drawings and the accompanying description.

Figure 2 shows an embodiment of the invention where two parallel control paths are used. The general blocks including envelope extractor **12**, control gain calculator **14**, control smoother **16**, and delay line **18** retain the same functionality as previously illustrated in Figure 1. The detailed internal structure of each block supports two parallel paths. The first path consists of a first envelope extractor **12-1**, a first control gain calculator **14-1**, and a first control smoother **16-1** and is designed to deliver limiting and dynamic range compression control gain. The second path consists of a second envelope extractor **12-2**, a second control gain calculator **14-2**, and a second control smoother **16-2**, and is designed to deliver low-level-expansion control gain. It is noted that a peak interpolator **12-3**, inside envelope extractor block **12**, feeds both the first

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envelope extractor **12-1** and the second envelope extractor **12-2**. Sharing of the same peak interpolator for the two paths is done for computational efficiency. It is also noted that a FIR filter smoothing **16-3** is used inside control smoother **16**, by applying the gains from control smoother **16-1** and control smoother **16-2**
 5 combined by a multiplier **16-4**.

As a non-limiting example, first envelope extractor **12-1** can be a recursive peak-envelope extractor, as described in the following algorithmic expression:

$$\text{if } Env(i-1) > \text{abs}(In(i)) \quad (1)$$

$$10 \quad Env(i) = tc * Env(i-1) + (1 - tc) * \text{abs}(In(i))$$

else

$$Env(i) = \text{abs}(In(i))$$

where:

$In(i)$ is the input to the envelope extractor at sample interval i ;

15 $Env(i)$ is the extracted envelope's value at sample interval i ; and

tc is a constant controlling the release time of the envelope extractor. In this case, a release time of about 10 milliseconds is appropriate.

As a non-limiting example, second envelope extractor **12-2** can be a recursive RMS-envelope extractor, such as described in the following algorithmic
 20 expression:

$$Env(i) = tc * Env(i-1) + (1 - tc) * \text{abs}(In(i)) \quad (2)$$

where:

$In(i)$ is the input to the envelope extractor at sample interval i ;

$Env(i)$ is the extracted envelope's value at sample interval i ; and

25 tc is a constant controlling the release time of the envelope extractor. In this case, a release time of about 100 milliseconds is appropriate.

Thus, the different task of limiting and compressing the dynamic range, and the task of low-level-expansion are each provided with suitable methods of

envelope extraction, each involving suitable response times.

Figure 3 illustrates the use of a family of compressor-limiter control curves, and is a graph of compressor-limiter control gain versus envelope according to the present invention. These graphs are suggested for the control gain calculator for the case of limiting and dynamic range compression, and are
 5 described by the following algorithmic expression:

$$g_1 = \frac{1}{1/\text{Gain} + (1 - 1/\text{Gain}) * \text{Env}} \quad (3)$$

where:

g_1 is the functional gain;

10 Env is an envelope input to the control gain calculator; and

Gain is a desired maximum gain.

Four curves are shown, corresponding to desired maximum Gain levels: a curve **30** for 24 dB, a curve **32** for 18 dB, a curve **34** for 12 dB, and a curve **36** for 6dB. As can be noted from the graphs, the general behavior of all these curves
 15 can be characterized as follows:

For envelope values lower than $1/\text{Gain}$ the curve asymptotically approaches the desired maximum gain Gain . In this range a gentle dynamic range compression of about 6dB takes place.

For envelope values in the range of about $1/\text{Gain}$ to $\sqrt{(1/\text{Gain})}$, the curve
 20 gradually lowers the gain. In this range most of the dynamic range compression takes place.

For envelope values of about $\sqrt{(1/\text{Gain})}$ to 1.0, the curve asymptotically approaches $1/\text{Env}$. In this range limiting takes place.

Due to their gradually changing character, these curves are suitable to
 25 perform both the limiting and dynamic range compression task, and even under very fast response time, will still allow for reasonable dynamics of the processed speech signal.

Figure 4 illustrates the use of a family of low-level expander control curves, and is a graph of low-level expander control gain versus envelope

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according to the present invention. These graphs are suggested for the control gain calculator in order to prevent excessive amplification of background noise, and are described by the following algorithmic expression:

$$g_2 = \text{minimum} (1.0, Env/Th) \quad (4)$$

5 where

Env is an envelope input to the control gain calculator; and

Th is a desired threshold below which gain should decrease.

Four curves are shown, corresponding to desired Threshold levels: a curve **40** for –42 dB, a curve **42** for –36 dB, a curve **44** for –30 dB, and a curve **46** for –
10 24 dB. As can be noted from the graphs, the general behavior of all these curves can be characterized as follows:

For envelope values above the Threshold, the gain is constant 1.0 (0 dB). This range is where the speech signal is expected.

As envelope values drop below the Threshold, the gain begins to decrease
15 at the same rate as does the envelope.

Due to the gradual decrease of gain below the Threshold, these curves cope well in situations where the actual speech signal happens to fall below the Threshold.

Figures 5A through 5C illustrate the use of a delay in the audio path to
20 allow for a look-ahead in the control path. Figure 5D illustrates the use of FIR filtering, and shows the effect of look-ahead, and look-ahead in combination with recursive or FIR filter smoothing, according to the present invention. The ability to precisely control peaks and Peak-to-RMS ratio is shown.

Precise control of the peaks of a speech signal requires instant response.
25 This requirement forces smoothing with short response time, and conflicts with the need to reduce audible distortions, which requires longer response times.

In order to be able to apply smoothing with longer response time, while still being able to precisely control the peaks, the concept of look-ahead is introduced. According to the present invention, the input signal path is delayed
30 relative to the control signal path. This is equivalent to allowing the control logic

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to look ahead in time, and to make adjustments for future changes in the input signal, prior to when the input arrives at the final output. Thus, introducing a delay into the input allows the use of control smoothing with slower response time while still achieving precise control of the peaks.

5 According to the invention, any kind of smoothing can be applied in order to take advantage of the look-ahead, such as infinite input response (IIR) recursive smoothing or linear phase FIR smoothing. While recursive smoothing is more efficient to implement, linear phase FIR smoothing can achieve more precise results. According to the present invention, therefore, in order to achieve
10 the best results, a linear phase FIR filter of order N should be used, where N exactly equals the number of delay samples in the look-ahead delay line. Also, the sum of all the FIR filter coefficients should equal 1.0. A practical example of such a filter is a simple running average of order N , as described below:

$$y(i) = (1/N) * (x(i) + x(i-1) + \dots + x(i-N+1)) \quad (5)$$

15 where:

$x(i)$ is the input to the filter at time i ,

$y(i)$ is the output of the filter at time i .

N is the FIR filter order.

Equation (5) may also be written in the form:

$$20 \quad y(i) = a_1 * x(i-N+1) + a_2 * x(i-N+2) + \dots + a_k * x(i-N+k) + \dots + a_N * x(i) \quad (6)$$

where the filter coefficients a obey the following condition:

$$a_1 + a_2 + \dots + a_k + \dots + a_N = 1 \quad (7)$$

An example for IIR recursive smoothing filter is:

$$25 \quad y(i) = tc * y(i-1) + (1 - tc) * x(i) \quad (8)$$

where:

$x(i)$ is the input to the filter at time i ,

$y(i)$ is the output of the filter at time i .

tc is a time constant controlling the response time of the filter. In this case

the response time should match the delay time introduced by the look-ahead delay line.

Figure 5A shows the unprocessed speech signal of the syllable 'plo' from the word 'plosives'. Featured are a speech signal **50** with an RMS **52**. It can be
5 seen that the peak-to-RMS ratio in this case is more than 12dB.

Figure 5B shows the same speech signal of Figure 5A processed with no look-ahead by the following processing chain: The recursive peak-envelope extractor of Equation (1), with a response time of 10 milliseconds, followed by the control gain calculator of Equation (3) above, using a Gain of 20dB, followed
10 by the recursive smoothing filter of Equation (8) above, using a time constant of 1 millisecond.

Figure 5C shows the same speech signal of Figure 5A processed by the processing chain as in Figure 5B but with a look-ahead of 1 millisecond.

Figure 5D shows the same speech signal of Figure 5A processed by the
15 processing chain as in Figure 5B but with a look-ahead of 1 millisecond, and using the FIR filter of Equation (5) above instead of the recursive smoothing filter of Equation (8).

It can be readily seen that in the case illustrated by Figure 5B, where no look-ahead was employed, the peaks at the beginning of the syllable (at around
20 $t = 0.03\text{ms}$) increased significantly, and the overall peak to RMS actually increased. Also the resulting signal exceeds the value ± 1.0 , reaching almost ± 2.0 , which will cause clipping. These problems arise since the smoothing with 1 millisecond response time does not allow the control gain to follow changes of the input signal fast enough.

25 In the case illustrated by Figure 5C, where the same smoothing filter is used, but with look-ahead, it can be seen that the peaks at the beginning are properly controlled and the overall peak-to-RMS is reduced. The resulting signal exceeds ± 1.0 only by a small, tolerable amount.

In the case illustrated by Figure 5D, where the FIR filter is used, the best
30 control over the peaks and the best peak-to-RMS are attained. The resulting

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signal does not exceed ± 1.0 .

It should be noted that the above smoothers could be cascaded with other types of smoothers that have instant attack time, without degrading the performance regarding peaks. In particular, since a slow release time after a peak is typically preferred, cascading a smoother having instant attack time and slow release time is desirable, because doing so will maintain the attack functionality while increasing the release time.

One example for such an instant attack, slow release smoother is described by the following algorithmic expression:

10 if $(x(i) > y(i))$ (9)
 $y(i) = y(i - 1) * tc + x(i) * (1 - tc)$
 else

$y(i) = x(i)$

 where:

15 $x(i)$ is the input control gain to the smoother at time i .

$y(i)$ is the resulting smoothed control gain at time i .

tc is a time constant in the range $0 < tc < 1$ that controls the release time.

Figure 6 illustrates the use of digital domain peak-interpolators for estimating the peaks of the input signal, and shows the effect of continuous domain peak estimation according to the present invention. In Figure 6 is a signal **60** representing the analog domain magnitude of a short section of the spoken consonant 's'. Signal **60** results from the conversion of a digital domain signal sampled at 8Khz. When a continuous signal is put into the digital domain by sampling, the peaks of the continuous signal may not be sampled precisely at their maximum value. Often the highest peaks of the continuous signal happen to fall in between two samples. In such cases, simply utilizing the peak values of the digital sample will not relate to the actual peaks of the corresponding continuous signal. It can be seen that the digital samples, indicated by the small circles in Figure 6, are often lower than the continuous analog signal peaks. For example,

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the value of an analog peak **62** is not accurately reflected in the value of a corresponding digital sample **64**, as indicated by the small circle. In most telephony applications it is the dynamic range of the analog circuitry that is of concern, so it is important to estimate the actual peak values of the continuous
 5 signal for precise peak control. It is possible to reconstruct the corresponding continuous domain signal from the digital samples by way of interpolation. In the above example, an estimated peak value **66**, as indicated by the asterisk, will result from interpolation. According to the present invention, any method of interpolation may be used for this purpose, such as the windowed Sinc
 10 interpolation filter. In a preferred embodiment of the present invention, several first-order IIR filters are used in parallel to estimate the continuous signal peaks. This configuration is illustrated in Figure 7, and is especially efficient to implement.

Figure 7 shows a block diagram for a peak estimator using all-pass filters
 15 according to the present invention. An input **70** feeds an all-pass filter **72**, an all-pass filter **74**, and an all-pass filter **76**. Absolute value detectors **78**, **80**, **82**, and **84** are fed by input **70**, all-pass filter **72**, all-pass filter **74**, and all-pass filter **76**, respectively. The outputs of absolute value detectors **78**, **80**, **82**, and **84** are input to a maximum value detector **86**, from which an output **88** is derived.
 20 All-pass filters **72**, **74**, and **76** apply different phase shifts to input signal **70** to produce phase-shifted input signals. In each sample period, the sample with the highest absolute magnitude among input **70** and all-pass filters **72**, **74**, and **76** is thus delivered as the output.

The first-order IIR all-pass filters have the general transfer function:

$$25 \quad H(z) = \frac{a + z^{-1}}{1 + az^{-1}} \quad (10)$$

For the example of Figure 6, the coefficients a used in the all-pass filters **72**, **74**, and **76** have the respective values 0.6682, 0.4142, and 0.1989.

In Figure 6, it can readily be seen that the peak estimates provided by the circuit of Figure 7 (indicated by the asterisks in Figure 6) matches much better the

peaks of the continuous signal than the raw digital samples (indicated by the small circles).

Additional Embodiments of the Present Invention

5 It is noted that the processing principles of the present invention can be applied at any point within an audio transmission or distribution system from the audio source to right before the final audio reproduction, or anywhere in between. Specifically, in case of telecommunications or other voice communications systems, the processing can be applied at the transmitting end, before
10 transmission, at the receiving end, before audio reproduction, or at any point of the telecommunication network between the transmitting and receiving end.

In systems with a local telephone switchboard, for example, the processing can be applied in the switchboard or within the telephones themselves for either receiving, transmitting, or both receiving and transmitting.

15 For a cordless telephone or mobile telephone that plugs into a base station (such as a cellular telephone, a "hands free" system used in cars, or a cordless home telephone), the processing can be applied within the handset or within the base station.

Other relevant embodiments include video conferencing, teleconferencing,
20 and so forth, such as illustrated in Figure 11, where multiple input signals are to be heard simultaneously. In such cases, processing according to the present invention can be performed for each signal individually, and at any point between the transmitting and receiving ends. Alternatively, the processing can be applied to the superposition of all input signals at a central location.

25 Similarly, in telephony applications, the present invention may be used with Voice over Internet Protocol and voice messaging (such as in various Unified Messaging systems). In such cases, processing can be performed at the transmitting end, the receiving end, or within the server.

Embodiments with Linked Processing of Multi-Channel Audio

It is noted that the present invention also applies where the input audio signal is supplied in a multi-channel format, such as in stereo or “surround sound” formats. In multi-channels audio formats the relative levels and phase
5 between the channels encodes spatial information about sound source localization. In order to preserve this information, it is desirable to maintain the relative levels and phase between the channels. As shown in Figure 8, for the case of N audio input channels **90**, instead of single delay line (such as delay line **18** in Figure 1), N delay lines **92** of the same length are used. Instead of single
10 multiplier (such as multiplier **20** Figure 1) N multipliers **94** are used, where each multiplier applies the same smoothed control signal to the respective delayed audio channel. Inside an envelope extractor **96**, the instantaneous maximum magnitude between all audio channels is detected and supplied as the input to the same kind of envelope detector to create a unified envelope of the N channels.
15 Subsequent processing is carried out in the same manner as in the single-channel case previously illustrated in Figure 1.

As illustrated in Figure 9 for the case of multi-channel audio where peak detection is needed, the peak detection has to be done individually for each channel by N peak interpolators **100**. Here, the instantaneous maximum
20 magnitude between all audio channels is detected, and supplied as the input to an envelope extractor **102** to create a unified envelope of the N channels. As before, subsequent processing is carried out as in the single-channel case previously illustrated in Figure 1.

The special case of stereo audio input with separate peak detection is
25 shown in Figure 10.

It is to be noted that in Figure 2, not all the illustrated components are necessarily present. For certain applications, a subset of the components can be sufficient. Omitting some of the components may be imposed by processing power limitations or for considerations of efficiency. Omitting some of the
30 components can lead to sub-optimal, but still satisfactory results. In a

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non-limiting example of the present invention, for control paths having a control gain calculator that operates only at low signal levels and applies principally to background noise (such as the gate control gain calculator), artifacts pertaining to audio quality are less critical. Thus, in some applications envelope detection may
5 be omitted from such control signal paths. Also, in such cases a common final smoother may be sufficient and the control smoother dedicated to this control path may be omitted. Examples of such configurations are shown in Figure 12 and Figure 13.

While the invention has been described with respect to a limited number of
10 embodiments, it will be appreciated that many variations, modifications and other applications of the invention may be made.

CLAIMS:

1. A voice signal processing system receiving an input signal characterized by at least one envelope, the system having an output signal and a specified maximum gain, the system comprising:

- 5 (a) an input for receiving the input signal;
- (b) an envelope extractor coupled to said input for extracting at least one envelope of the input signal;
- (c) a control gain calculator coupled to said envelope extractor, for calculating at least one gain, wherein said control gain calculator is operative to performing a calculation taken from the group containing:
- 10 i) a first gain calculation of $\frac{1}{1/Gain + (1 - 1/Gain) * Env}$, wherein Env is said envelope and $Gain$ is the specified maximum gain;
- ii) a second gain calculation of the minimum of 1.0 and Env/Th , wherein Th is a threshold below which the result of said second gain calculation decreases; and
- 15 iii) the product of said first gain calculation and said second gain calculation;
- (d) a control smoother coupled to said control gain calculator for smoothing said at least one gain, and for delivering as the output signal a control gain;
- 20 (e) a delay line coupled to said input, to produce a delayed input; and
- (f) an output multiplier coupled to said delay line and to said control smoother for applying said control gain to said delayed input.

25 2. The system according to Claim 1, wherein:

- (a) the input signal is in the time domain and has peaks; and

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- (b) at least one of said envelope extractors includes a peak interpolator in the digital domain for estimating said peaks of the input signal.
3. The system according to Claim 2, wherein said peak interpolator includes:
- (a) at least one all-pass filter coupled to said input for delivering at least one phase-shifted input signal having a magnitude; and
- 5 (b) a selector for selecting said phase-shifted input signal having the greatest magnitude.

4. The system according to Claim 1, wherein:
- (a) at least one of said control smoothers includes at least one linear phase FIR filter of order N , for smoothing said at least one gain;
- 10 (b) said delay line has a delay measured in sample periods;
- (c) said order N equals the length of said delay in said sample periods; and
- (d) said linear phase FIR filter is operative to performing a calculation of
- 15

$$y(i) = a_1 * x(i - N + 1) + a_2 * x(i - N + 2) + \dots \\ + a_k * x(i - N + k) + \dots + a_N * x(i)$$

where:

- (a) said $y(i)$ is the output of said linear phase FIR filter at a time i ;
- 20 (b) said $x(i)$ is the input to said linear phase FIR filter at said time i ;
- (c) said a_1, a_2, \dots, a_k , and a_N are coefficients of said linear phase FIR filter; and
- (d) $a_1 + a_2 + \dots + a_k + \dots + a_N = 1$.

5. A method for processing a voice signal characterized by at least one envelope, the method resulting in an output signal characterized by a specified maximum gain, the method comprising the steps of:
- 25

- (a) receiving the voice signal;

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- (b) extracting at least one envelope of the voice signal;
- (c) performing a calculation taken from the group containing:
- i) a first gain calculation of $\frac{1}{\frac{1}{Gain} + (1 - \frac{1}{Gain}) * Env}$, wherein Env is said envelope and $Gain$ is the specified maximum gain;
 - 5 ii) a second gain calculation of the minimum of 1.0 and Env/Th , wherein Th is a threshold below which the result of said second gain calculation decreases; and
 - iii) the product of said first gain calculation and said second gain calculation;
- 10 (d) smoothing said at least one gain, and delivering as the output signal a control gain;
- (e) delaying the voice signal to produce a delayed input; and
- (f) multiplying said delayed input by said control gain.
6. The method according to Claim 5, wherein the input signal is in the time domain and has peaks, the method further comprising the step of:
- 15 (g) estimating said peaks of the input signal by digital domain peak interpolation.
7. The method according to Claim 6, further comprising the steps of:
- (h) shifting the phase of the input signal to produce at least one phase-shifted input signal having a magnitude; and
 - 20 (i) selecting said phase-shifted input signal having the greatest magnitude.
8. The method according to Claim 5, wherein said delayed input has a delay measured in sample periods, and wherein smoothing said at least one gain includes the step of filtering said at least one gain by performing the calculation
- 25

$$y(i) = a_1 * x(i - N + 1) + a_2 * x(i - N + 2) + \dots + a_k * x(i - N + k) + \dots + a_N * x(i)$$

– 20 –

where:

- (a) N is the length of said delay in said sample periods;
- (b) said $y(i)$ is the output of said filtering at a time i ;
- (c) said $x(i)$ is the input to said filtering at said time i ;
- 5 (d) said a_1, a_2, \dots, a_k , and a_N are coefficients; and
- (e) $a_1 + a_2 + \dots + a_k + \dots + a_N = 1$.

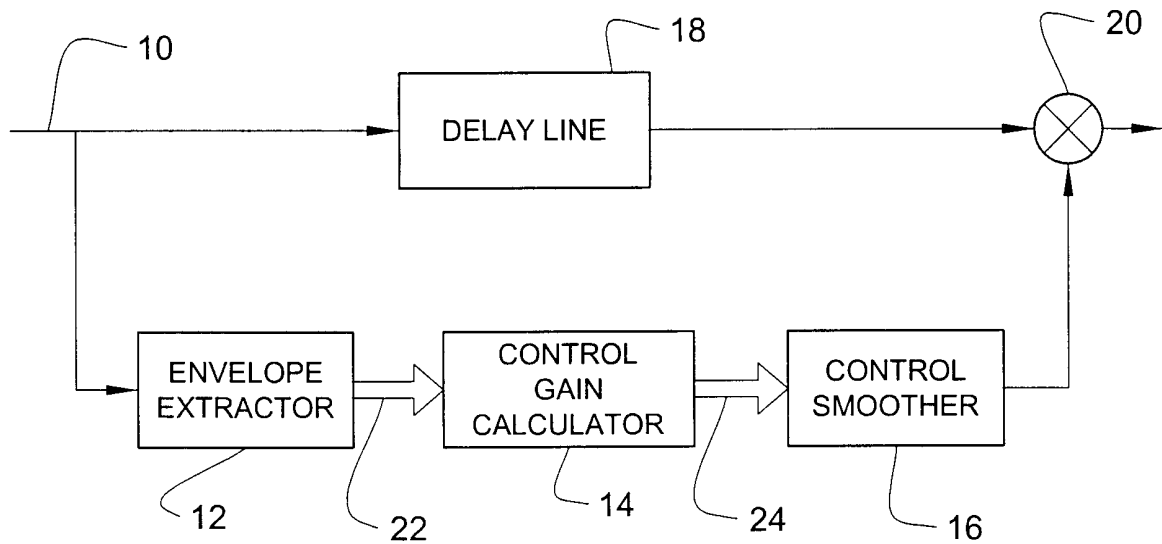


FIG. 1

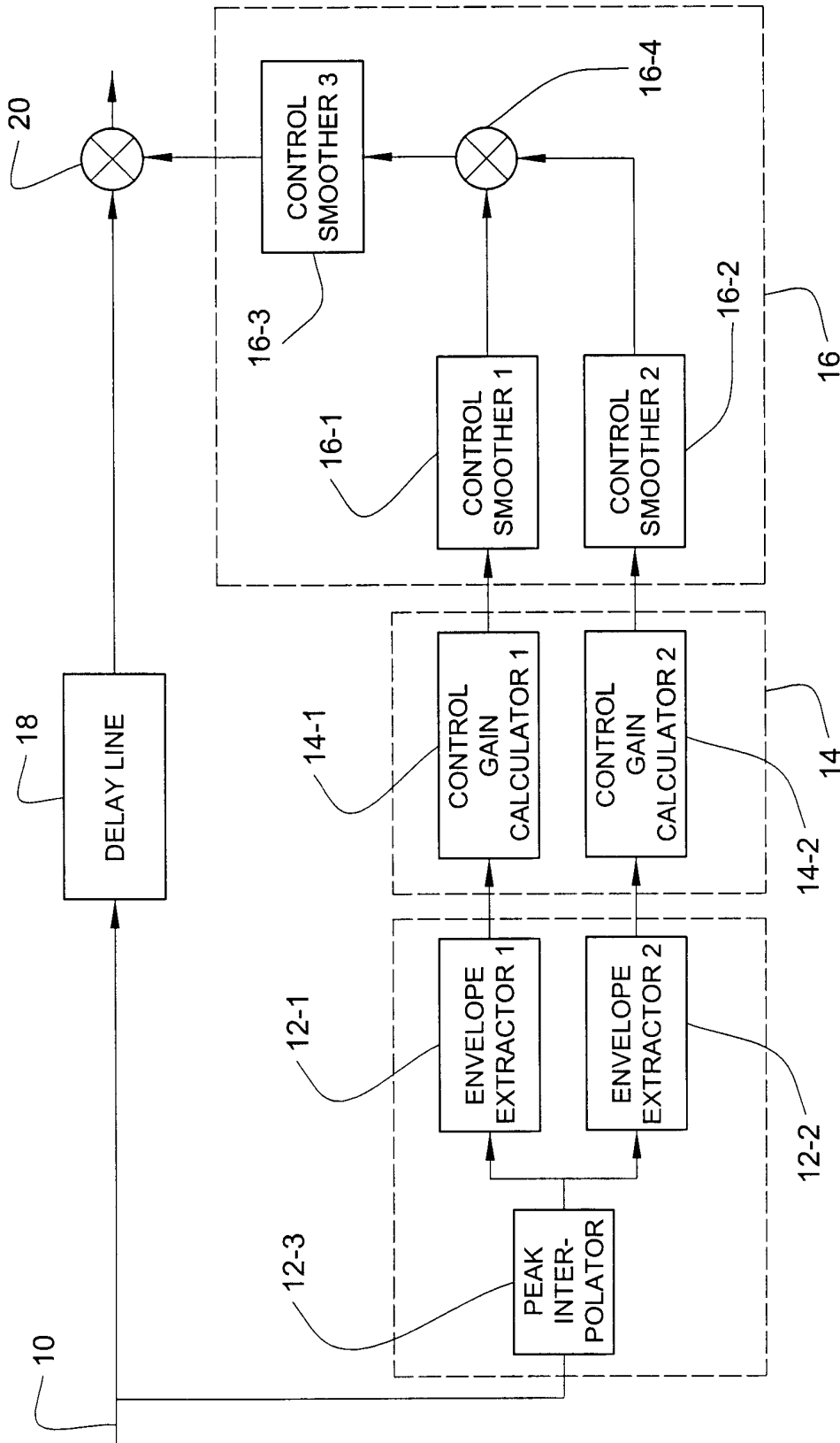


FIG. 2

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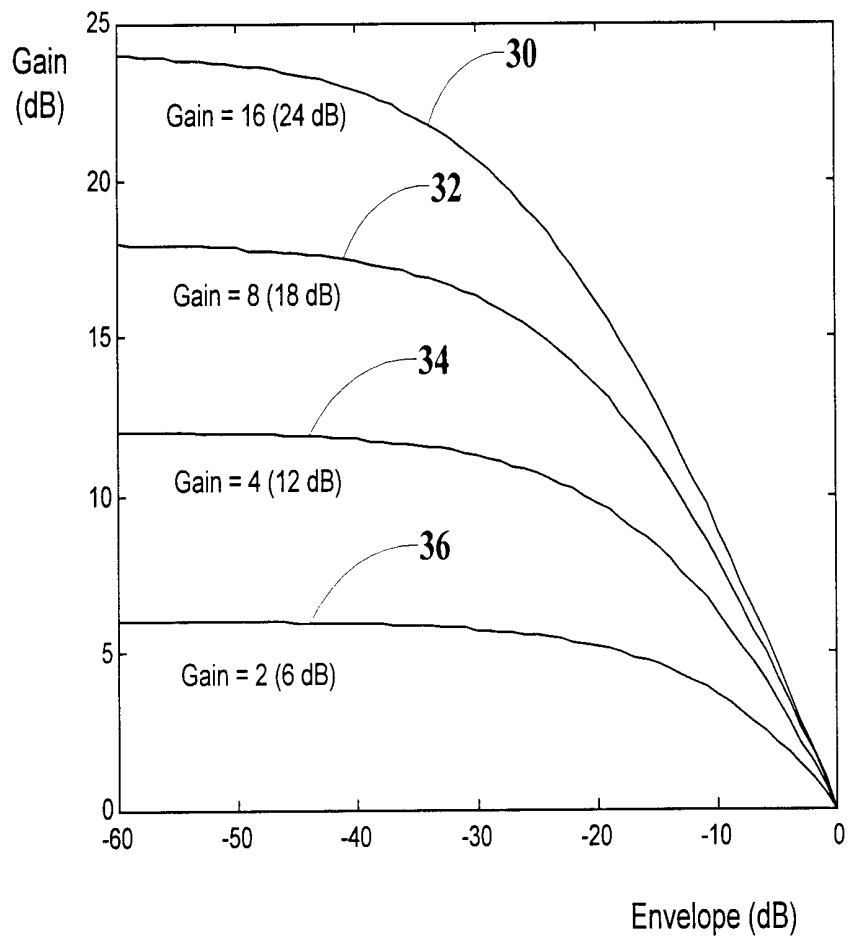


FIG. 3

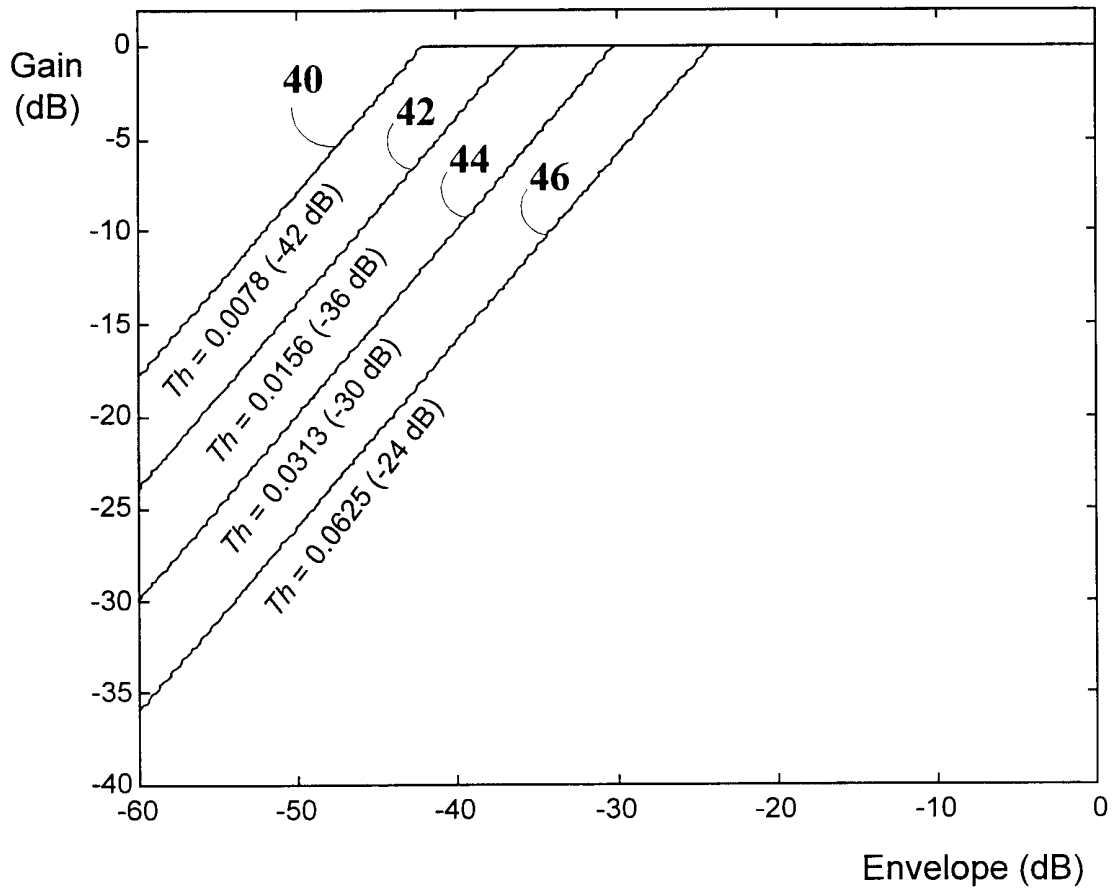


FIG. 4

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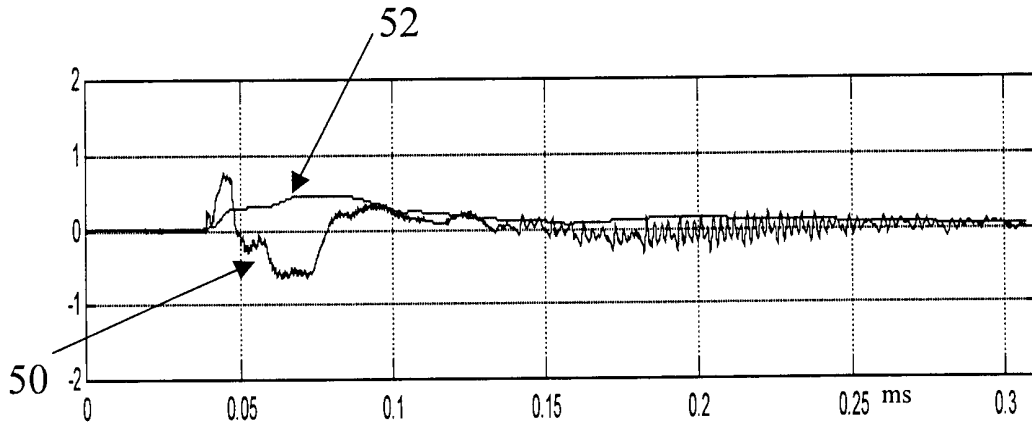


FIG. 5A

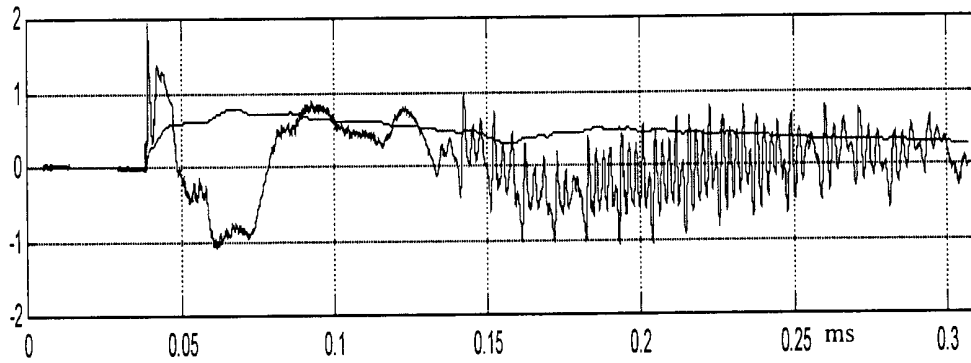


FIG. 5B

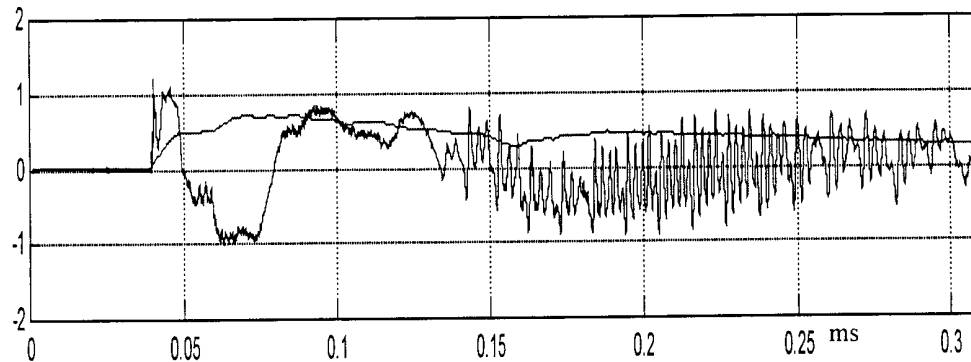


FIG. 5C

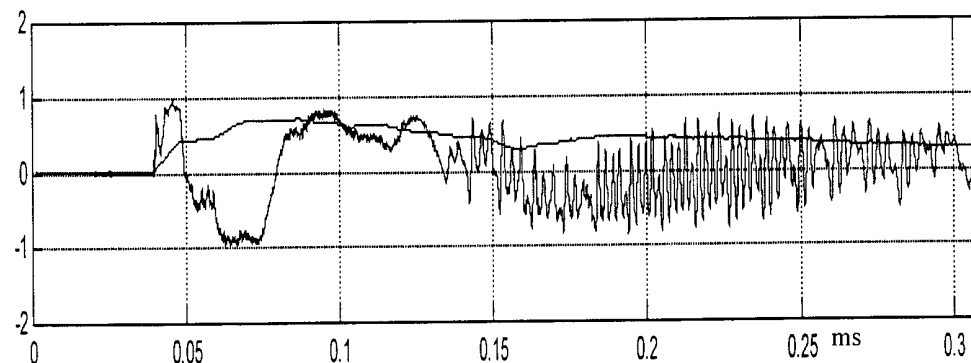


FIG. 5D

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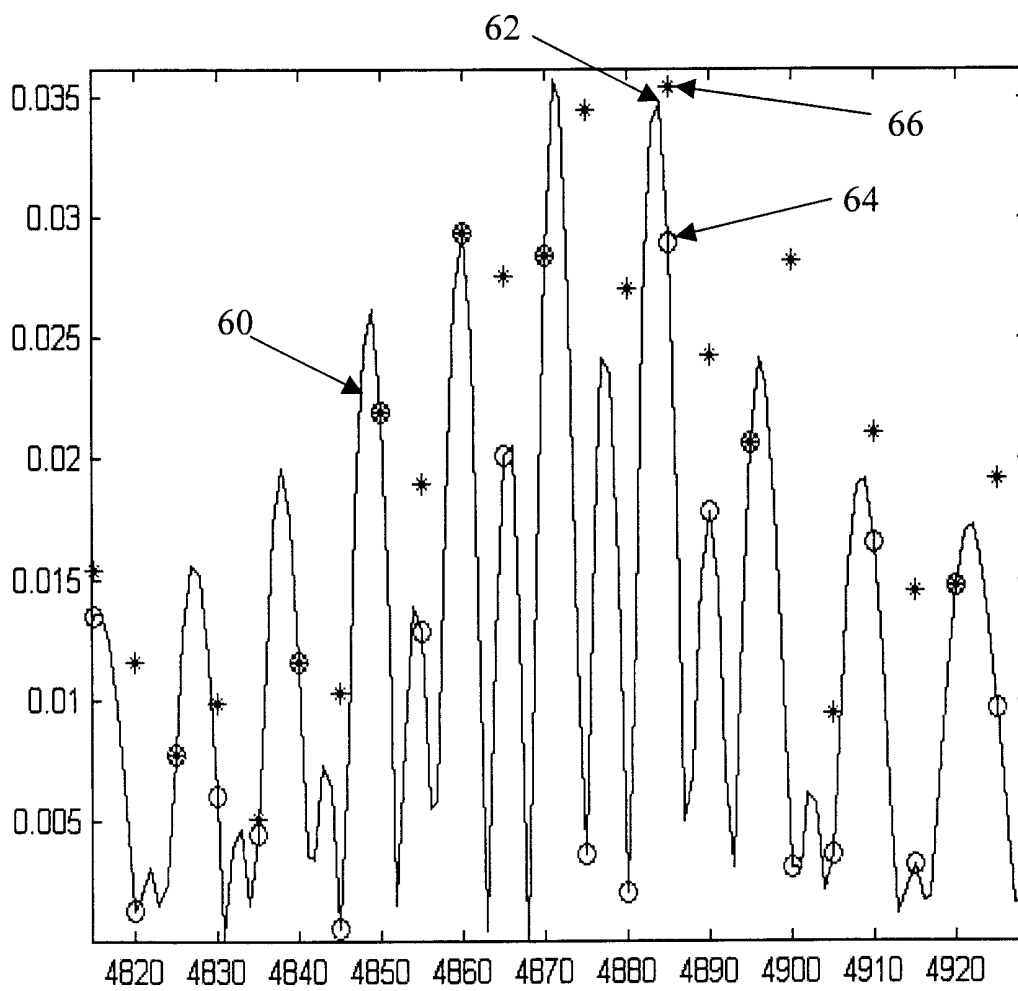


FIG. 6

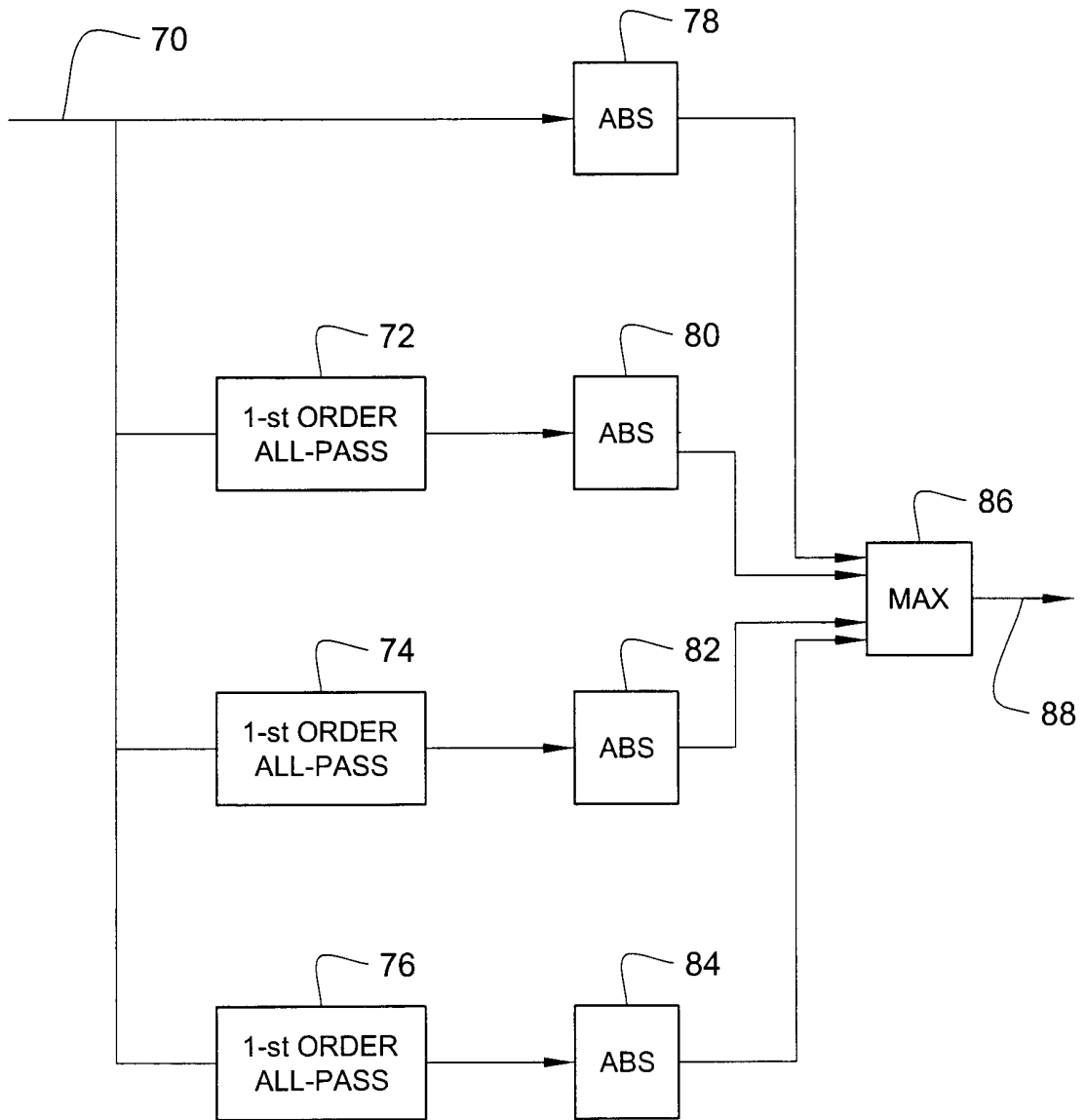


FIG. 7

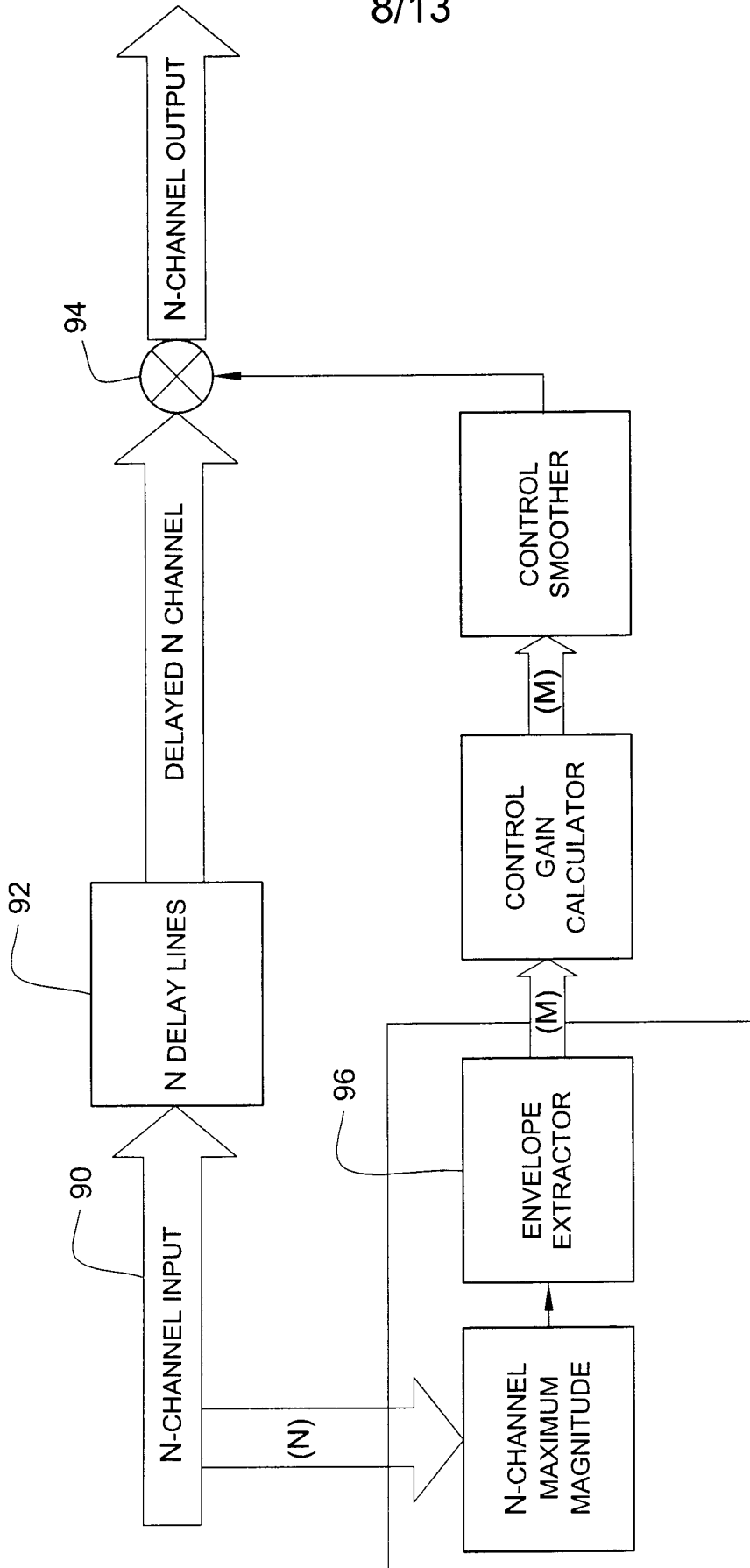


FIG. 8

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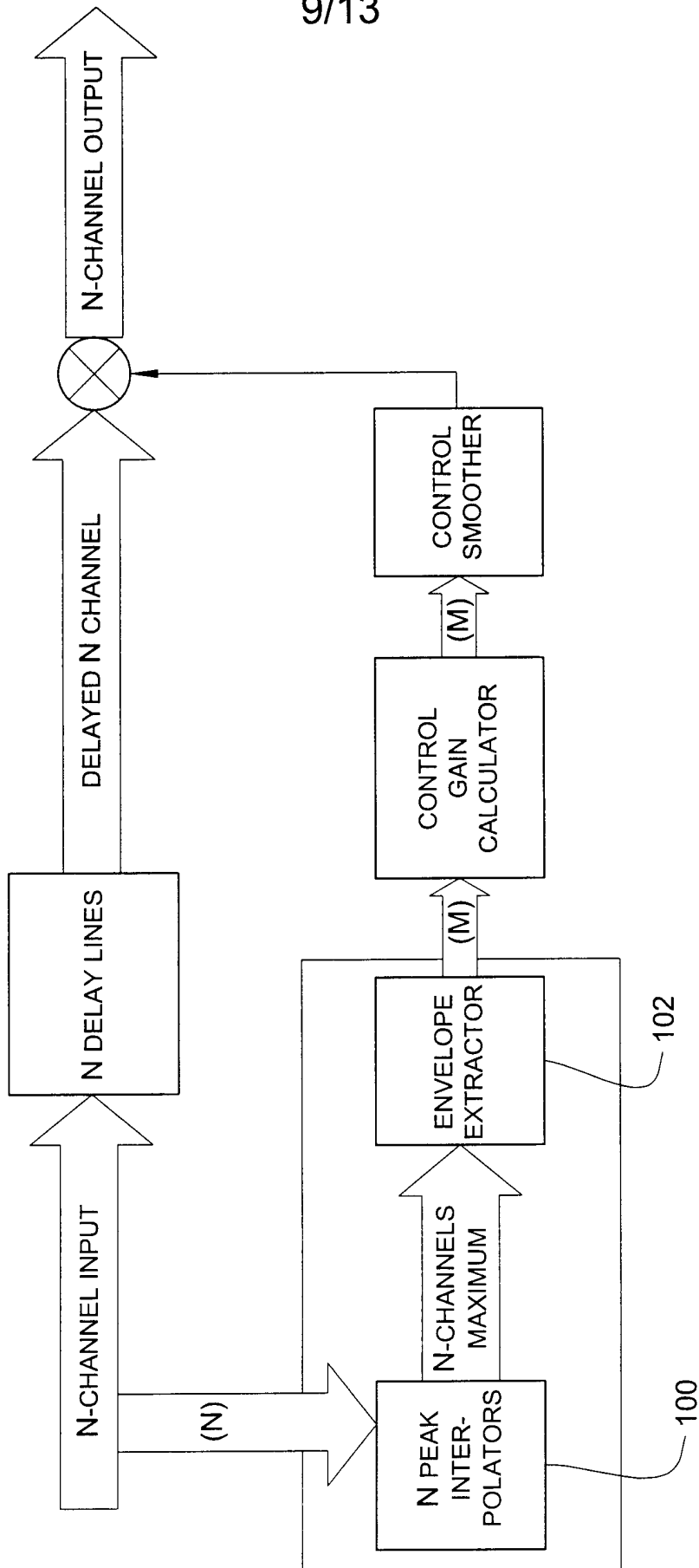


FIG. 9

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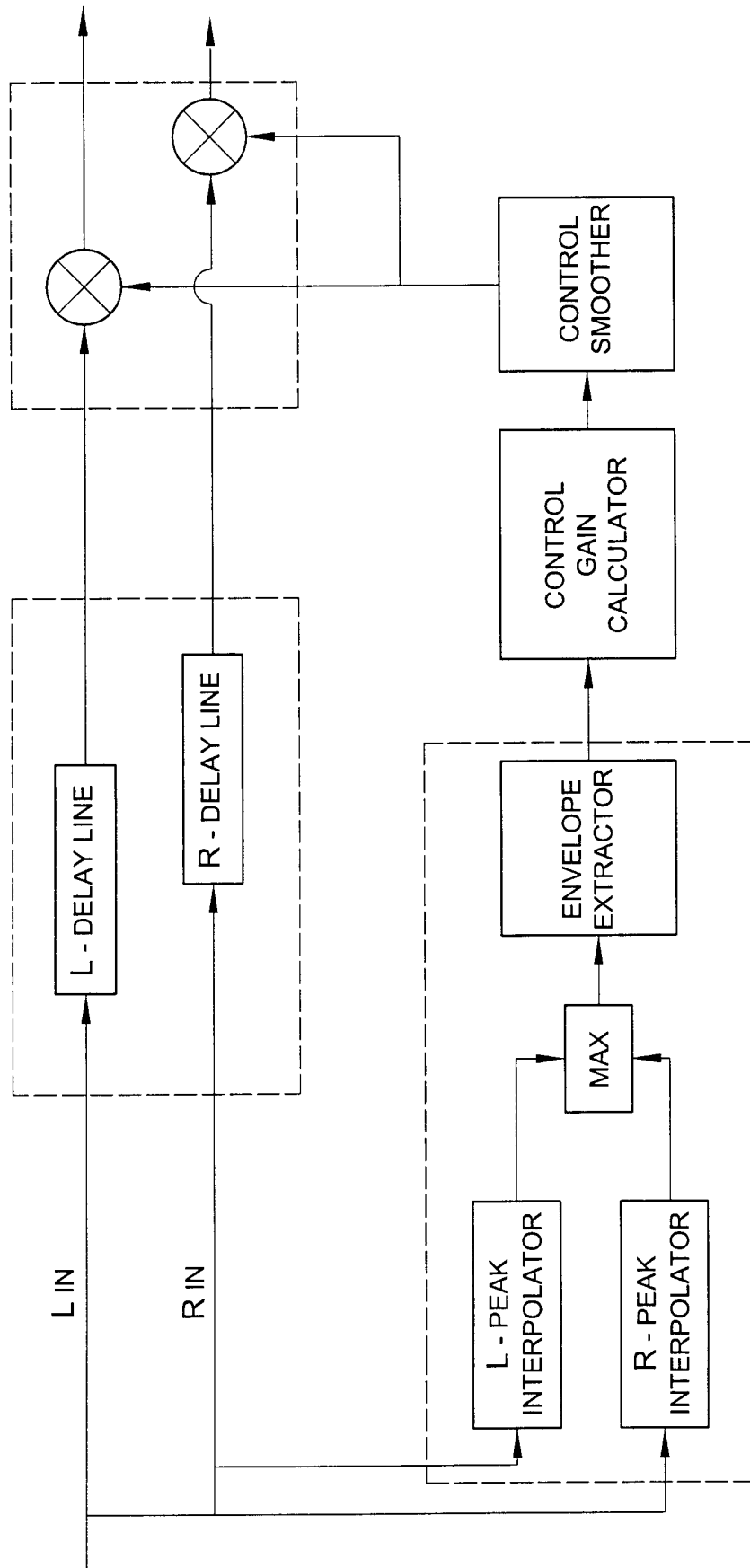


FIG. 10

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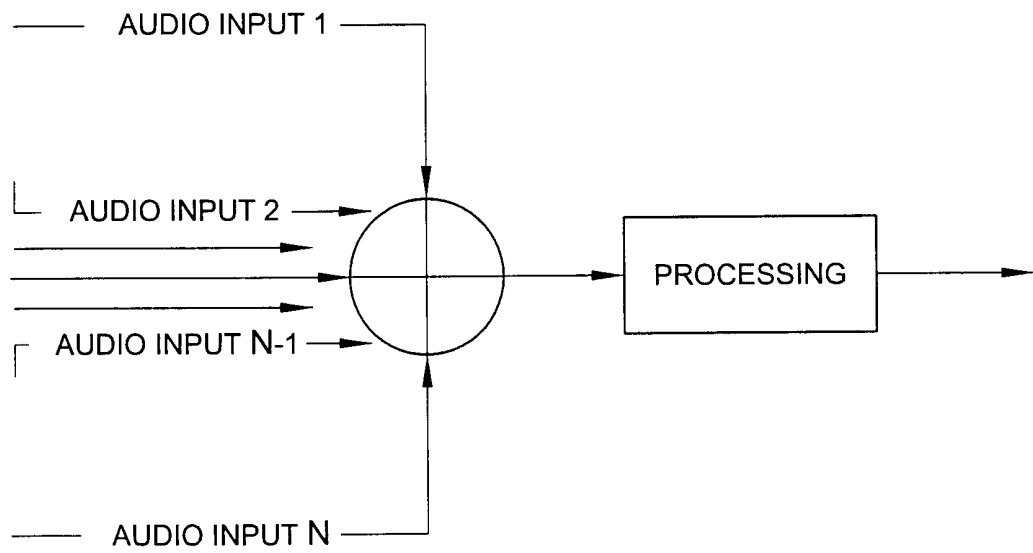


FIG. 11

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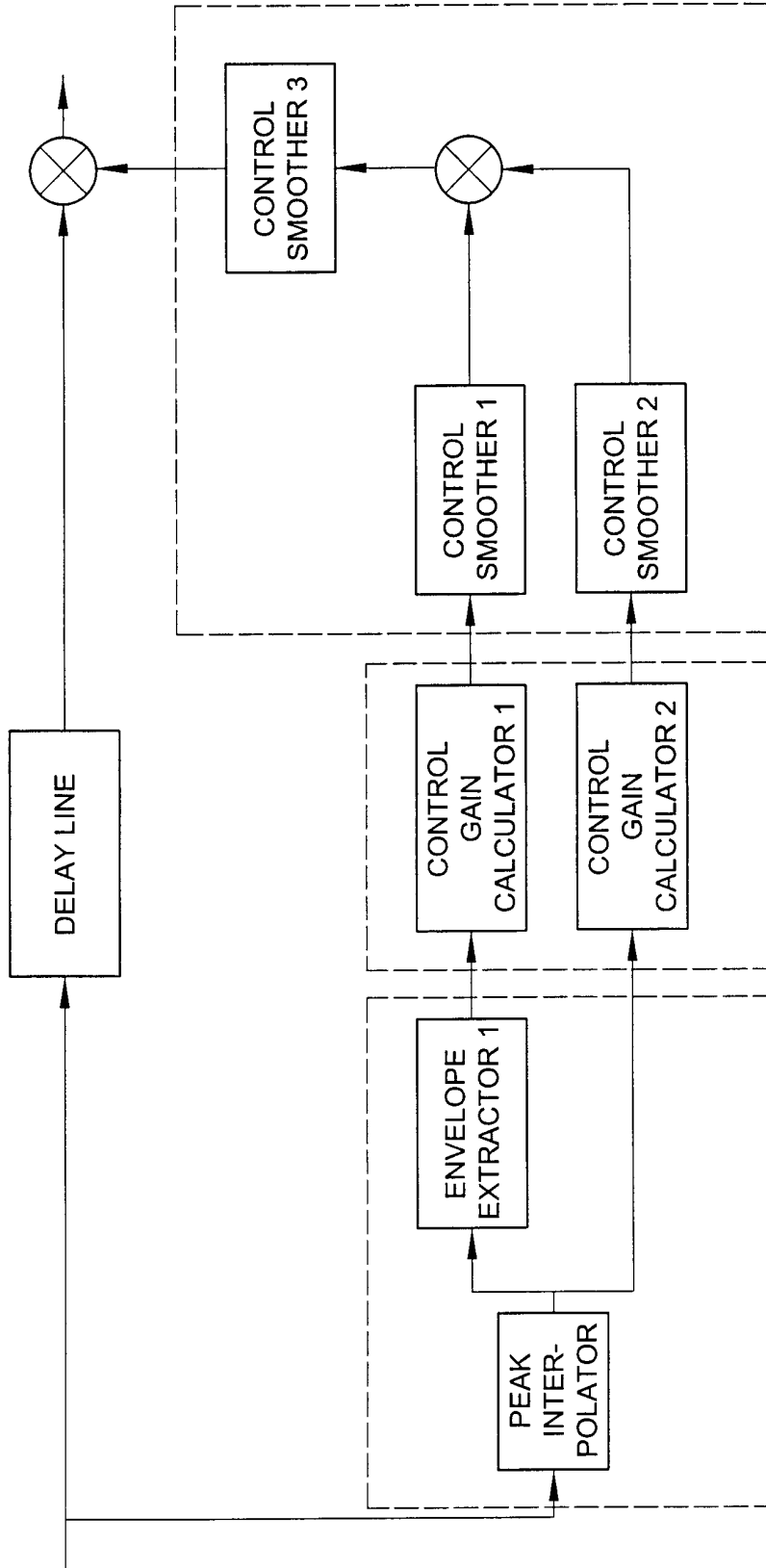


FIG. 12

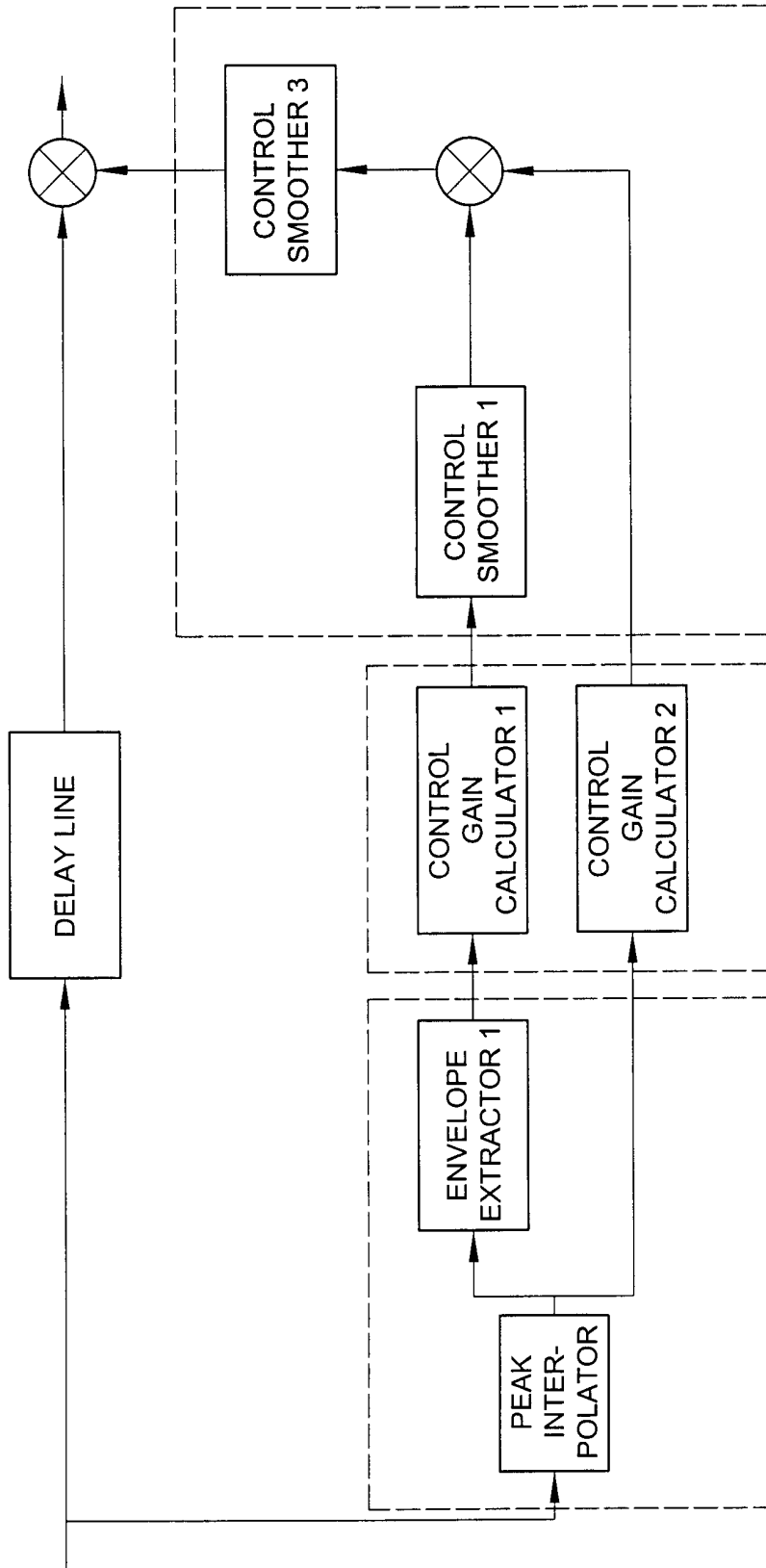


FIG. 13

INTERNATIONAL SEARCH REPORT

International Application No

PCT/IL 00/00580

A. CLASSIFICATION OF SUBJECT MATTER
IPC 7 H03G7/00

According to International Patent Classification (IPC) or to both national classification and IPC

B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)
IPC 7 H03G

Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched

Electronic data base consulted during the international search (name of data base and, where practical, search terms used)

EPO-Internal, INSPEC, PAJ

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category *	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	EP 0 763 888 A (NOKIA MOBILE PHONES LTD) 19 March 1997 (1997-03-19) column 5, line 23 -column 7, line 21; figures 3-5	1,5
A	GB 2 000 945 A (DOLBY LAB LICENSING CORP) 17 January 1979 (1979-01-17) abstract	1,5
A	US 5 784 476 A (BIRD NEIL C) 21 July 1998 (1998-07-21) column 4, line 36 -column 5, line 25; figure 4	1,5

Further documents are listed in the continuation of box C.

Patent family members are listed in annex.

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Date of the actual completion of the international search

23 November 2000

Date of mailing of the international search report

30/11/2000

Name and mailing address of the ISA

European Patent Office, P.B. 5818 Patentlaan 2
NL - 2280 HV Rijswijk
Tel. (+31-70) 340-2040, Tx. 31 651 epo nl,
Fax: (+31-70) 340-3016

Authorized officer

Blaas, D-L

INTERNATIONAL SEARCH REPORT

Information on patent family members

International Application No

PCT/IL 00/00580

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