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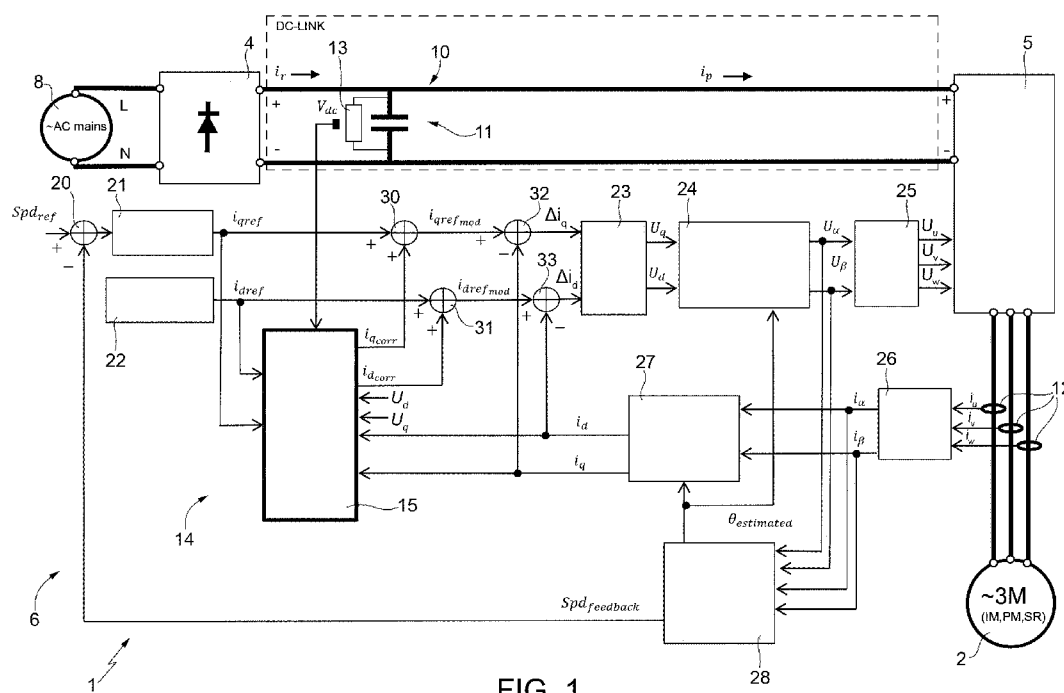


FIG. 1

(57) **Abstract:** Inverter-based apparatus (1) configured to control an electric motor (2), the inverter-based apparatus comprising: an input stage (4) configured to convert an alternating voltage AC to a rectified DC voltage; an electrolytic-capacitor-less inverter (5) configured to generate an AC voltage to be fed to said electric motor (2) based on duty cycles of switching signals; a DC-link (10) connecting said electrolytic-capacitor-less inverter (5) to the input stage (4) and crossed by an instantaneous active power (P(t)) from, or towards, said electrolytic-capacitor-less inverter (5); a DC-link capacitor (11) connected to said DC-link (10); voltage sensor (13) configured to determine the amplitude of said DC-link capacitor voltage (Vdc(t)); current sensors (12) configured to determine the amplitude of output currents applied to said electric motor (2) by said electrolytic-capacitor-less inverter (5); a current regulator system (14) configured to control said duty cycles based on determined current references (idref, iqref); and an active voltage limiter unit

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(15) configured in order to determine an active current (i_a)(i_{aref}) associated to the instantaneous active power ($P(t)$) absorbed from, or supplied back, said DC-link (10), and regulate said current references (i_{dref} , i_{qref}) based on said active current (i_a)(i_{aref}).

INVERTER BASED APPARATUS AND CONTROL METHOD THEREOF

The present invention relates to an inverter based apparatus and control method thereof. More specifically, the present invention relates to an inverter based apparatus
5 configured to operate a motor, in particular a permanent magnet motor or an induction motor or any other similar motor, of an household appliance, such as, for example, a washing machine, a drying machine, a refrigerator and/or dish washer and/or air conditioner. It is understood that according to the present invention, the inverter controlling method and apparatus are designed to control a motor associated to any
10 kind of load of a household appliance, such as, for example, a drum, a compressor, a fan, a pump, etc..

As is known, nowadays inverters driving motors are widely applied to home appliances. In general, an inverter driving motor comprises an input stage and an inverter bridge, which is provided, in turn, with a plurality of switching units, which
15 are controlled in order to generate and modulate an AC voltage to be fed to motor terminals. The input stage generally comprises a diode bridge having inputs coupled to mains for receiving the AC mains voltage, outputs for providing a DC voltage, and an electrolytic capacitor for removing voltage ripples which appear in rectified voltage.

Depending on the power size, the inverters for home appliances are usually
20 configured in order to have a high capacitance so as to keep the ripple voltage, and thus a ripple current, within a reasonable level, generally comprised between 10% to 15%. Indeed the electrolytic capacitor worsen the life expectation if the ripple voltage/current increases, and a small ripple voltage is recommended for a seamless drive of the motor. However, if on the one side a flat and stable DC voltage across
25 capacitor, i.e. low ripple voltage, improves the performance of motor driving algorithms, on the other side it affects the mains current by harmonics.

In order to solve such problem, inverters for home appliances are usually provided with a power factor corrector unit (active or passive) which comprises an inductor having enough inductance to increase the power factor (thus the harmonics)
30 to the desired value. However, factor corrector unit has the disadvantage to be an

expensive and bulky component.

Aim of the present invention is to solve the drawbacks referred above.

In compliance with the above aims, according to the present invention there is provided an inverter-based apparatus configured to control an electric motor, the
5 inverter-based apparatus comprising: an input stage which is connected to mains lines for receiving AC lines currents and AC mains voltage and configured to convert said AC mains voltage to a rectified DC voltage; an electrolytic-capacitor-less inverter, which is configured to generate output currents to be fed to said electric motor based on duty cycles of switching signals; a DC-link which connects said electrolytic-
10 capacitor-less inverter to the input stage and is crossed by DC-link currents from, or towards, said electrolytic-capacitor-less inverter; a DC-link capacitor connected to said DC-link; a voltage sensor configured to determine the amplitude of said DC-link capacitor voltage; one or more current sensors configured to determine the amplitude of output currents provided to said electric motor by said electrolytic-capacitor-less
15 inverter, and a current regulator system which is configured to control said duty cycles based on determined current references and said output currents, the inverter-based apparatus further comprises an active voltage limiter unit, which is configured to regulate said current references of said current regulator system in order to limit said DC-link capacitor voltage within a predetermined voltage range.

20 Preferably, the active voltage limiter unit is further configured to regulate said current references of said current regulator system without using said lines currents and/or DC-link currents and/or the current of the DC capacitor.

Preferably, said active voltage limiter unit is further configured to clamp said DC-link capacitor voltage to a prefixed value, when said electric motor regenerates
25 back current to said the DC-link capacitor via said electrolytic-capacitor-less inverter.

Preferably, said active voltage limiter unit is further configured to determine an active current based on said output currents and said duty cycles, and regulate said current references based on said active current and said DC-link capacitor voltage.

Preferably, said active voltage limiter unit is configured to determine a first
30 active current based on the d-q axis-wise duty cycles indicative of said duty cycles of

the switching signals and d-q axis-wise currents indicative of said output currents.

Preferably, said active voltage limiter unit is configured to determine a second active current based on the d-q axis-wise duty cycles indicative of said duty cycles of the switching signals and said current references.

5 Preferably, said active voltage limiter unit is configured to determine said active current, by computing the minimum between said first and second active currents.

Preferably, said active voltage limiter unit is configured to determine two maximum absolute correction signals on the basis of said second active current and
10 said d-q axis-wise duty cycles.

Preferably, said active voltage limiter unit is configured to determine an instantaneous maximum allowable regeneration current based on a measured voltage level and a parameter indicative of a maximum absolute active current for regeneration.

15 Preferably, the active voltage limiter unit is configured to determine an instantaneous maximum allowable regeneration current $i_{aIstAbs}(t)$ based on the following equation

$$i_{aIstAbs}(t) = w_V(t) i_{aMaxAbs}$$

20

wherein where $w_V(t)$ is a time-varying weight that depends on the measured capacitor voltage $V_{dc}(t)$ and the nominal DC-link voltage V_{dcnom} and on the high-voltage limit V_{high} .

Preferably, said active voltage limiter unit is configured to determine
25 unconstrained axis-wise corrections to the reference currents as a fraction of the maximum correction by the following equation:

$$\begin{aligned} i_{dunc}(t) &= \rho(t) i_{dmax}(t) \\ i_{qunc}(t) &= \rho(t) i_{qmax}(t) \end{aligned}$$

30 where the time-varying weight $\rho(t)$ is determined according to an empirical saturated-

cubic equation:

$$\rho(t) = \text{sat} \left[\left(\frac{i_{a_{ws}}(t) + i_{a_{IstAbs}}(t)}{i_{a_{IstAbs}}(t)} \right)^3 \right]_{-1}^0$$

5 Preferably, said active voltage limiter unit is configured to determine constrained axis-wise current corrections by applying the following saturation and correction equations

$$i_{q_{corr}}(t) = \begin{cases} \max(i_{q_{unc}}(t), 0), & \text{if } \omega(t) > 0 \\ \min(i_{q_{unc}}(t), 0), & \text{if } \omega(t) < 0 \end{cases}$$

$$i_{d_{corr}}(t) = \min(i_{d_{unc}}(t), 0) - K_{qd} \text{abs}(i_{q_{corr}}(t) - i_{q_{unc}}(t))$$

wherein K_{qd} is a positive tuning gain that may be used to transfer to the d-axis part
15 of the correction originally computed for the q-axis, when saturation occurs.

Preferably, said active voltage limiter unit is configured to modify said current references according to the following equations:

$$i_{d_{refMod}}(t) = i_{d_{ref}}(t) + i_{d_{corr}}(t)$$

$$i_{q_{refMod}}(t) = i_{q_{ref}}(t) + i_{q_{corr}}(t)$$

20

The present invention further relates to a control method implemented by an inverter-based apparatus configured to control an electric motor, wherein said inverter-based apparatus comprises: an input stage which is connected to mains lines for receiving AC lines currents and AC mains voltage and configured to convert said alternating mains voltage AC to a rectified DC voltage; an electrolytic-capacitor-less
25 inverter, which is configured to generate output currents to be fed to said electric motor based on duty cycles of switching signals; a DC-link which connects said electrolytic-capacitor-less inverter to said input stage and is crossed by DC-link currents from, or towards, said electrolytic-capacitor-less inverter; a DC-link capacitor connected to

said DC-link; a voltage sensor configured to determine the amplitude of said DC-link capacitor voltage; one or more current sensors configured to determine the amplitude of output currents provided to said electric motor by said electrolytic-capacitor-less inverter; and a current regulator system which is configured to control said duty cycles
5 based on determined current references and said output currents; said control method being characterized by regulating said current references of said current regulator system in order to limit said DC-link capacitor voltage within a predetermined voltage range.

So, more generally, the present invention relates also to a method for
10 controlling an electric motor by an apparatus comprising an input stage to convert an AC mains voltage to a rectified DC voltage, an electrolytic capacitor-less inverter connected to the input stage by a DC-link, and a capacitor connected to the DC-link, the method comprising the following steps:

- generating, by the electrolytic capacitor-less inverter, output currents to be fed
15 to the electric motor based on duty cycles of switching signals;
- determining the output currents fed to the electric motor;
- controlling the duty cycles based on current references and the determined output currents;
- determining the voltage across the capacitor; and
- 20 • regulating the current references so as to limit the capacitor voltage within a predetermined voltage range.

Preferably, the control method comprises regulating said current references of said current regulator system without using said lines currents and/or any DC-link currents and/or the current of the DC capacitor.

25 Preferably, the control method comprises the step of clamping said DC-link capacitor voltage to a prefixed value, when said electric motor regenerates back current to said the DC-link capacitor via said electrolytic-capacitor-less inverter.

Preferably, the control method comprises the step of determining an active current based on said output currents and said duty cycles; regulating said current
30 references based on said active current and said DC-link capacitor voltage.

Preferably, the method comprises the step of determining a first active current based on the d-q axis-wise duty cycles indicative of said duty cycles of the switching signals and d-q axis-wise currents indicative of said output currents.

Preferably, the method comprises the steps of determining a second active
5 current based on the d-q axis-wise duty cycles indicative of said duty cycles of the switching signals and said current references.

Preferably, the method comprises the step of determining said active current, by computing the minimum between said first and second active currents.

Preferably, the method comprises the step of determining two maximum
10 absolute correction signals on the basis of said second active current and said d-q axis-wise duty cycles.

Preferably, the method comprises determining an instantaneous maximum allowable regeneration current based on a measured voltage level and a parameter indicative of a maximum absolute active current for regeneration.

15 Preferably, the method comprises the step of determining an instantaneous maximum allowable regeneration current $iaIstAbs(t)$ based on the following equation

$$i_{aIstAbs}(t) = w_V(t) i_{aMaxAbs}$$

20 wherein where $w_V(t)$ is a time-varying weight that depends on the measured capacitor voltage $Vdc(t)$ and the nominal DC-link voltage $Vdcnom$ and on the high-voltage limit $Vhigh$.

Preferably, said active voltage limiter unit is configured to determine unconstrained axis-wise corrections to the reference currents as a fraction of the
25 maximum correction by the following equation:

$$\begin{aligned} i_{dunc}(t) &= \rho(t) i_{dmax}(t) \\ i_{qunc}(t) &= \rho(t) i_{qmax}(t) \end{aligned}$$

where $\rho(t)$ is a time-varying weight determined according to an empirical saturated-
30 cubic equation:

$$\rho(t) = \text{sat} \left[\left(\frac{i_{a_{ws}}(t) + i_{a_{IstAbs}}(t)}{i_{a_{IstAbs}}(t)} \right)^3 \right]_{-1}^0$$

5 Preferably, the method comprises the step of determining constrained axis-wise current corrections by applying the following saturation and correction equations

$$10 \quad i_{q_{corr}}(t) = \begin{cases} \max(i_{q_{unc}}(t), 0), & \text{if } \omega(t) > 0 \\ \min(i_{q_{unc}}(t), 0), & \text{if } \omega(t) < 0 \end{cases}$$

$$i_{d_{corr}}(t) = \min(i_{d_{unc}}(t), 0) - K_{dq} \text{abs}(i_{q_{corr}}(t) - i_{q_{unc}}(t))$$

Wherein K_{dq} is a positive tuning gain that may be used to transfer to the d-axis part
15 of the correction originally computed for the q-axis, when saturation occurs.

Preferably, the method comprises the step of modifying said current references according to the following equations:

$$20 \quad \begin{aligned} i_{d_{refMod}}(t) &= i_{d_{ref}}(t) + i_{d_{corr}}(t) \\ i_{q_{refMod}}(t) &= i_{q_{ref}}(t) + i_{q_{corr}}(t) \end{aligned}$$

A non-limiting embodiment of the present invention will now be described, by way of example, with reference to the accompanying drawings, in which:

- Figure 1 is a block diagram of an inverter-based apparatus provided according to the present invention; and
- 25 – Figure 2 is a flow chart of operation implemented by an active voltage limiter unit.

With reference to Figure 1, reference number 1 denotes as a whole an inverter-based apparatus 1 configured to control an electric motor 2 according to the control method disclosed hereinafter. Preferably, the electric motor is a three-phase motor 2,
30 but it can be any kind of multi-phases motor 2, such as bi-phase or poly-phases motor,

or similar motor. Moreover, the electric motor 2 may be a permanent magnet motor or an induction motor or any other similar motor.

According to a preferred embodiment, the electric motor 2 may be comprised in a household appliance (not illustrated). The household appliance may be, for example, a washing machine, and/or a drying machine, or a refrigerator, or a dish washer, or an air conditioner, or any similar domestic machine. Preferably, the inverter-based apparatus 1 is configured to control an electric motor 2 associated to a component/load of the household appliance such as, for example, a drum, a compressor, a fan, a pump, or any other device/element of the household appliance driven by the electric motor 2.

With reference to Figure 1, the inverter-based apparatus 1 comprises an input stage 4, an inverter 5 and a motor controller stage 6.

According to an exemplary embodiment illustrated in Figure 1, the input stage 4 comprises a rectifier unit configured to convert an alternating voltage AC, received in input from a power supply system 8, to a rectified DC voltage to be provided in input to the inverter 5. The input stage 4 may comprise, for example, a full-bridge diode rectifier having inputs coupled to AC mains lines of the power supply system 8 for receiving AC mains lines currents and AC mains voltage, and outputs connected to the inverter 5. It is understood that both power supply system 8 and input stage 4 depend on the kind of inverter and motor to be controlled. For example, power supply system 8 and input stage 4 may be three-phases, or multi-phases, or similar.

According to an exemplary embodiment illustrated in Figure 1, the inverter 5 is configured to convert the DC voltage to AC voltage. The inverter 5 may be provided with a plurality of switching units (not illustrated), which are controlled by the motor controller stage 6 in order to generate and modulate an AC voltage to be fed to the motor 2. In the exemplary embodiment, the inverter 5 comprises inputs connected to outputs of the input stage 4 to receive the DC voltage and outputs connected to the electric motor 2.

According to a preferred embodiment, the rectifier unit of the input stage 4 comprises a single-phase rectification circuitry, while the inverter 5 comprises a three-

phase inverter having two inputs connected to respective outputs of the rectifier unit and three outputs connected to respective terminals of the electric motor 2.

With reference to Figure 1, the inverter-based apparatus 1 further comprises a DC-link 10, in turn comprising two DC-link lines, connecting the outputs of the input stage 4 with the inputs of the inverter 5, a capacitor 11, a current sensor 12, and a voltage sensor 13. The DC-link capacitor 11 is connected between the two DC-link lines of the DC-link 10, i.e. between the outputs terminals of the input stage 4. Conveniently, the DC-link capacitor 11 may have a capacitance comprised between about 1 μ F and about 2 μ F. The Applicant has found that using a DC-link capacitor 11 with low-capacitance has the technical effect of increasing the ripple voltage up to 100% so to have a very good harmonic content in the mains current, which allows to eliminate the power factor corrector unit.

In other words, using the DC-link capacitor 11 with low-capacitance has the advantage of removing any expensive and bulky power factor corrector circuit specifically designed for correction of harmonics (such as an inductor coupled in series between the mains output and the diode bridge input), since, due to the small capacitance of the DC-link capacitor 11, the rectified current still has a substantial harmonic content. Preferably, the DC-link capacitor 11 may comprise a film type capacitor. The film type capacitor is conveniently less expensive and more durable compared to an electrolytic capacitor. Since the inverter 5 does not comprise an electrolytic capacitor, it corresponds to an “electrolytic-capacitor-less inverter”.

The current sensor 12 can be configured to sense the output currents of the inverter 5 applied to the electric motor 2. With reference to exemplary embodiment illustrated in Figure 1, current sensor 12 may comprise one or more sensors configured to sense the currents provided to the three-phase motor 2, i.e. phase currents $i_u(t)$, $i_v(t)$, $i_w(t)$. It is understood that the time-dependence of the currents $i_u(t)$, $i_v(t)$, $i_w(t)$ is not illustrated in Figures the sake of clarity.

The voltage sensor 13 is preferably configured to sense the voltage $V_{dc}(t)$ of the DC-link capacitor 10.

With reference to Figure 1, the motor controller stage 6 may comprise a current

regulator system 14 and an active voltage limiter unit 15.

The current regulator system 14 is configured to receive information on the sensed currents $i_u(t)$, $i_v(t)$, $i_w(t)$ from the current sensor 12, receive information on the sensed voltage $V_{dc}(t)$ from the voltage sensor 13, receive information on a motor control parameter i.e. a requested motor speed Spd_{ref} provided by an appliance control unit (not illustrated), and to generate three signals $U_u(t)$, $U_v(t)$, $U_w(t)$ to control the switching units of the inverter 5.

The signals $U_u(t)$, $U_v(t)$, $U_w(t)$ may be indicative of duty cycles of the command signals provided to the switching units of the inverter 5. The signals $U_u(t)$, $U_v(t)$, $U_w(t)$ may be also per-unit signals indicative of the fraction of DC-link voltage to be applied to each phase of the motor. The three signals $U_u(t)$, $U_v(t)$, $U_w(t)$ may be pulse width modulation signals (PWM).

According to an embodiment shown in Figure 1, the current regulator system 14 may comprise: an subtractor stage 20, a speed control stage 21, a flux weakening stage 22, a currents regulator stage 23, an inverse-Park transform stage 24, an inverse-Clarke convert stage 25, a direct-Clarke convert stage 26, a direct-Park transform stage 27, and a sensorless speed/flux position observer stage 28.

The direct-Clarke convert stage 26 is configured to convert the three-phase sensed currents $i_u(t)$, $i_v(t)$, $i_w(t)$ into a two-phase α, β Park-coordinate system (stationary reference frame), and provide current values $i_\alpha(t)$ and $i_\beta(t)$ to the direct-Park transform stage 27 and to the sensorless speed/flux position observer stage 28.

The sensorless speed/flux position observer stage 28 is configured to receive the three-phase sensed currents $i_u(t)$, $i_v(t)$, $i_w(t)$ and two signals $U_\alpha(t)$ and $U_\beta(t)$. The signals $U_\alpha(t)$ and $U_\beta(t)$ are indicative of two duty cycles values in the two-phase α, β Park-coordinate system. The sensorless speed/flux position observer stage 28 is further configured to provide a rotor speed signal $Spd_{feedback}$ relating to the actual speed of the rotor, based on the three-phase sensed currents $i_u(t)$, $i_v(t)$, $i_w(t)$ and the signals $U_\alpha(t)$ and $U_\beta(t)$. The sensorless speed/flux position observer stage 28 is further configured to provide an angle $\theta_{estimated}$ indicative of the rotor angle estimated, based on the three-phase sensed currents $i_u(t)$, $i_v(t)$, $i_w(t)$. In an exemplary

embodiment, the sensorless speed/flux position observer stage 28 may comprise a rotor angular position estimator and rotor angular speed estimator. The rotor angular position estimator may be configured to determine the angular position $\theta_{estimated}$ of the rotor based on the sensed currents $i_u(t)$, $i_v(t)$, $i_w(t)$ without using a position sensor,
 5 whereas the rotor angular speed estimator may be configured to determine the rotor speed $Spd_feedback$ based on the angular position $\theta_{estimated}$.

The Park transform stage 27 is configured to receive the angle $\theta_{estimated}$ and the measured current values i_α and i_β in the two-phase α, β Park-coordinate system (stationary reference frame) and to convert the current values $i_\alpha(t)$ and $i_\beta(t)$ to a two-
 10 phase d-q coordinate system (rotating-synchronous reference frame), generating the measured synchronous currents $i_d(t)$ and $i_q(t)$ based on the angle $\theta_{estimated}$.

In the exemplary embodiment, the subtractor stage 20 is configured to receive in input a motor speed signal Spd_ref and the motor speed $Spd_feedback$. The motor speed signal $Speed-ref$ relates to a reference motor speed associated to a command
 15 signal indicating the requested motor speed, whereas the motor speed signal $Spd_feedback$ relates to the determined motor speed provided by the sensorless speed/flux position observer stage 28. The subtractor stage 20 is configured to determine a speed error based on the difference between input motor speed signals Spd_ref and $Spd_feedback$.

20 The speed control stage 21 is configured to receive the speed error and provide the current i_{qref} . For example, the speed control stage 21 may comprise a PI controller and is configured to operate in the two-phase d-q coordinate system. The current i_{qref} is indicative of the reference rotor current in the q-axis of the d-q coordinate system. The signals Spd_ref and $Spd_feedback$, i_{qref} and i_{dref} can be, in general, time-varying
 25 signals, whose explicit time dependence is not illustrated in the notation to improve clarity of the description.

The flux weakening stage 22 is configured to operate in the two-phase d-q coordinate system and to generate a reference current i_{dref} being indicative of the reference rotor current in the d-axis of the d-q coordinate system.

30 With regard to the active voltage limiter unit 15, it is configured to regulate the

current references supplied to the current regulator system 23 in order to limit the DC-link capacitor voltage $V_{dc}(t)$ within a predetermined voltage range.

Preferably, the active voltage limiter unit 15 is configured to regulate the current references for the I_d - I_q current regulators based on the DC-link capacitor voltage $V_{dc}(t)$ and the measured current values $i_d(t)$ and $i_q(t)$. Conveniently, the active voltage limiter unit 15 is configured to regulate the current references for the I_d - I_q current regulators without using any current measurement in the DC-link. In other words, the inverter-based apparatus 1 does not comprise any current sensor on the DC-link 10.

Preferably, the active voltage limiter unit 15 is configured to receive in inputs: the current reference i_{qref} , the current reference i_{dref} , the voltage $V_{dc}(t)$ of the DC-link capacitor 11, two signals $U_q(t)$ and $U_d(t)$ indicative to the duty cycles in a q-d coordinate system (hereinafter disclosed in detail) and the measured current values $i_d(t)$ and $i_q(t)$. The active voltage limiter unit 15 is further configured to determine two constrained axis-wise current corrections $i_{qcorr}(t)$ and $i_{dcorr}(t)$ by implementing the control method hereinafter disclosed in detail.

With reference to Figure 1, the current regulator system 14 further comprises an adder unit 30, an adder unit 31, a subtracting unit 32 and a subtracting unit 33.

The adder unit 30 is configured to receive the current reference i_{qref} and the q-axis-wise current correction $i_{qcorr}(t)$ and to provide in output a modified current reference $i_{qrefmod}(t)$ based on the addition of the current reference i_{qref} and the current correction $i_{qcorr}(t)$.

The adder unit 31 is configured to receive the current reference i_{dref} and the d-axis-wise current correction $i_{dcorr}(t)$ and to provide in output a modified current reference $i_{drefmod}(t)$ based on the addition of the current reference i_{dref} and the current correction $i_{dcorr}(t)$.

The subtracting unit 32 is configured to receive the modified current reference $i_{qrefmod}(t)$ and the measured current $i_q(t)$ and to provide in output the current difference $\Delta i_q(t)$ between the modified current reference $i_{qrefmod}(t)$ and the current $i_q(t)$.

The subtracting unit 33 is configured to receive the modified current reference $idrefmod(t)$ and the measured current $id(t)$ and to provide in output the current difference $\Delta id(t)$ between the modified reference current $idrefmod$ and the current id .

The currents regulator stage 23 is configured to receive in input the current difference $\Delta iq(t)$ and the current difference $\Delta id(t)$ and to provide in output the signals $Uq(t)$ and $Ud(t)$ respectively based on $\Delta iq(t)$ and $\Delta id(t)$. Signals $Uq(t)$ and $Ud(t)$ are indicative of the duty cycles in q-d coordinate system. Signals $Uq(t)$ and $Ud(t)$ may also be indicative of the fraction of maximum voltage to be applied along each axis of the synchronous d-q reference frame.

The inverse-Park transform stage 24 is configured to receive in input the signals $Uq(t)$ and $Ud(t)$ and to produce the signals $U\alpha(t)$ and $U\beta(t)$ indicative of the duty cycles values in the two-phase α , β Park-coordinate system. The signals $U\alpha(t)$ and $U\beta(t)$ may also be indicative of the fraction of maximum voltage to be applied along each axis of the stationary α - β reference frame.

The inverse-Clarke convert stage 25 is configured to receive in input the signals $U\alpha(t)$ and $U\beta(t)$ and to provide the switching signals $Uu(t)$, $Uv(t)$, $Uw(t)$ to the inverter unit 5.

Figure 2 is a flow chart of an exemplary control method that may be implemented by means of the active voltage limiter unit 15 (shown in Figure 1). In the exemplary embodiment, the active voltage limiter unit 15 is configured to implement the control method to control the current regulator system 14 in order to limit the voltage $Vdc(t)$ of the DC-link capacitor 11 during a regeneration mode as well as the minimum voltage during high-torque demands within a predetermined voltage range .

In this respect, the control method implemented by the active voltage limiter unit 15 uses a control parameter/signal, indicated hereinafter as estimated “active current $ia(t)$ ” (estimated from available and motor phase-currents and commanded duty-cycle signals to the inverter), and the voltage $Vdc(t)$ of the DC-link capacitor 11 to determine the current correction values $iqcorr(t)$ and $idcorr(t)$ to be used to modify the current references $iqref$ and $idref$ that current regulator system 14 uses to control the electric motor 2.

Control method performed by the active voltage limiter unit 15 controls the voltage $V_{dc}(t)$ of the DC-link capacitor 11 in order to “clamp” the voltage $V_{dc}(t)$ to a constant value in case, for example, the electric motor 2 tends to regenerate back-current ($i_p(t)$ becomes negative) to the DC-link capacitor 10 (i.e. during breaking of the motor). The situation of negative DC-link current $i_p(t) < 0$ can be detected through the computation of the said active current $i_a(t)$, that surrogates the unavailable current $i_p(t)$. Consequently, the method controls $i_{qrefmod}$ and $i_{drefmod}$ in order to limit the negative active current $i_a(t)$ till bringing it to zero if necessary (to completely cancel any back-current to the capacitor).

It will be disclosed hereinafter the meaning of the active current $i_a(t)$ used by the control method. Tests performed by Applicant proved that the dynamic of the DC-link capacitor 11 evolves according to the following equation:

$$\frac{d}{dt} V_{dc}(t) = \frac{i_r(t) - i_d(t)}{C_{dc}}$$

When the input stage 4 is a passive uncontrolled rectifier, then the current $i_r(t) > 0$ (current that flows from the rectifier to the DC-link capacitor) is uncontrollable (and fluctuates at twice the mains frequency) and, for the small capacitance of the DC-link capacitor 11, when $i_r(t)$ by chance approaches zero, even a small negative $i_p(t)$ (regeneration current occurring in braking operation) may cause a large voltage overshoot. This situation may harm the electronic components of the motor controller stage 6, which may fail due to overvoltage.

In this respect, the control method uses the active current $i_a(t)$, which is obtained by combining the measurements of the phase currents with the duty cycle commands, to detect the regeneration (i.e., the occurrence of back-currents). Indeed the active current $i_a(t)$ can be shown by algebraic formalism to correspond to a scaled version of the current $i_p(t)$, that is, the active current $i_a(t)$ can be used in place of the current $i_p(t)$ to detect regeneration and then to take provisions to limit the capacitor voltage $V_{dc}(t)$.

More specifically, in order to improve the clarity and facilitate the

understanding of the present invention, but without this implying any loss of generality, it will be described hereinafter how the active current $ia(t)$ controlled by the method according to the present invention relates to the current $ip(t)$.

The instantaneous active power $P(t)$, that is the power absorbed from (if $P(t) > 0$) or supplied back to (if $P(t) < 0$) the DC-link, may be expressed in terms of DC-link quantities:

$$\text{Equation (1)} \quad P(t) = V_{dc}(t)i_p(t)$$

The instantaneous current $ip(t)$ absorbed from (if $ip(t) > 0$) or supplied back/regenerated to the DC-link capacitor (if $ip(t) < 0$), can be computed by inverting equation (1) :

$$\text{Equation (2)} \quad i_p(t) = \frac{P(t)}{V_{dc}(t)}$$

The active power $P(t)$ can also be expressed in terms of the phase currents and voltages of the motor (referred to the motor's neutral point) by the scalar product:

$$\text{Equation (3)} \quad P(t) = V_u(t)i_u(t) + V_v(t)i_v(t) + V_w(t)i_w(t)$$

wherein, by using the dq0-Park's transformation:

$$\text{Equation (4)} \quad T(\theta) = \frac{2}{3} \begin{bmatrix} \cos(\theta) & \cos(\theta - \frac{2\pi}{3}) & \cos(\theta + \frac{2\pi}{3}) \\ -\sin(\theta) & -\sin(\theta - \frac{2\pi}{3}) & -\sin(\theta + \frac{2\pi}{3}) \\ \frac{1}{2} & \frac{1}{2} & \frac{1}{2} \end{bmatrix}$$

the active power can be expressed in terms of the d-q frame currents and voltages according to the following equation

$$\text{Equation (5)} \quad \begin{bmatrix} i_d(t) \\ i_q(t) \end{bmatrix} = T(\theta(t)) \begin{bmatrix} i_u(t) \\ i_v(t) \\ i_w(t) \end{bmatrix},$$

$$5 \quad \begin{bmatrix} U_d(t) \\ U_q(t) \end{bmatrix} = T(\theta(t)) \begin{bmatrix} U_u(t) \\ U_v(t) \\ U_w(t) \end{bmatrix},$$

$$P(t) = \frac{3}{2} \left(V_d(t)i_d(t) + V_q(t)i_q(t) \right) + 3V_0i_0.$$

10 Neglecting the zero-sequence current and voltage (V_0, i_0), the following simplified form for the active power is considered:

$$\text{Equation (6)} \quad P(t) = \frac{3}{2} \left(V_d(t)i_d(t) + V_q(t)i_q(t) \right)$$

15 Considering that voltages $V_d(t)$ and $V_q(t)$ are applied through a standard Space Vector Modulation switching strategy, they relate to the duty cycles $U_d(t)$ and $U_q(t)$ [PU] by

$$\text{Equation (7)} \quad \begin{aligned} V_d(t) &= \frac{1}{\sqrt{3}} V_{dc} U_d(t) \\ V_q(t) &= \frac{1}{\sqrt{3}} V_{dc} U_q(t) \end{aligned}$$

20 then it results in:

$$\text{Equation (8)} \quad i_p(t) = \frac{\sqrt{3}}{2} \left(U_d(t)i_d(t) + U_q(t)i_q(t) \right)$$

By defining the active current $i_a(t)$:

25

$$\text{Equation (9)} \quad i_a(t) := U_d(t)i_d(t) + U_q(t)i_q(t),$$

the signal can be computed by synchronous-frame currents and signals $U_d(t)$ and $U_q(t)$. Moreover, the following linear relation holds:

Equation (10)
$$i_p(t) = \frac{\sqrt{3}}{2} i_a(t).$$

Therefore, Applicant has found that controlling the active current $i_a(t)$, in view
 5 of Equation (10), is equivalent to controlling $i_p(t)$. In particular, zeroing $i_a(t)$
 corresponds to nullifying $i_p(t)$.

In case harmful regeneration is detected (negative $i_a(t)$ or increasing capacitor
 voltage $V_{dc}(t)$) then, as a first provision, it is possible to stop the regeneration current
 by nullifying $i_a(t)$.

10 Besides $i_a(t)$, it is possible to use another synthetic signal, named $i_{aref}(t)$, that
 gives an anticipation (forecast) on what will be the value of the active current $i_a(t)$
 after the current regulators have settled. Indeed, in a motor drive with current-
 regulators (for $i_d(t)$ and $i_q(t)$), the currents are commanded to prescribed values i_{dref}
 and i_{qref} , and the regulators are in charge of obtaining the required currents by
 15 computing suitable duty cycles, to be actuated by the inverter unit.

For a prescribed pair of reference currents, it is defined the-reference-active
 current-at-time-t, the signal computed with the reference currents and the duty cycles
 at time t:

20 Equation (11)
$$i_{aref}(t) := U_d(t)i_{dref} + U_q(t)i_{qref}$$

For a change in the reference currents (commanded in turn by a speed/torque
 controller or by a flux/weakening or magnetization block), the signal $i_{aref}(t)$ gives
 coarse forecast about what will be the active current after the transitory, since the
 25 current regulators will drive the currents toward the references.

Flow chart of Figure 2 contains the operations performed by the active voltage
 limiter unit 15 to modify the current references of the current regulator system 14 in
 order to limit the voltage $V_{dc}(t)$ of the DC-link capacitor 11 during regeneration mode,
 for example caused by braking or by an external sudden decrease of the load torque.

30 Firstly, the control method performs the step of determining the instantaneous

active currents $i_a(t)$ and $i_{aref}(t)$ based on: the duty cycles $U_d(t)$, $U_q(t)$, the available currents $i_d(t)$, $i_q(t)$ and the current references i_{dref} , i_{qref} (block 100) (using the axis d and q of the Clark transformation matrices).

Preferably, the control method determines the instantaneous active currents
5 $i_a(t)$ and $i_{aref}(t)$ by the formulas:

$$\begin{aligned} \text{Equation (12a)} \quad i_a(t) &= U_d(t)i_d(t) + U_q(t)i_q(t) \\ i_{aref}(t) &= U_d(t)i_{dref}(t) + U_q(t)i_{qref}(t) \end{aligned}$$

It is understood that the active current can be computed alternatively resorting
10 to currents and duty cycles in a reference frame different from the synchronous one, for instance using quantities expressed in the synchronous reference frame α - β , when available.

$$\begin{aligned} \text{Equation (12b)} \quad i_\alpha(t) &= U_\alpha(t)i_\alpha(t) + U_\beta(t)i_\beta(t) \\ i_{aref}(t) &= U_\alpha(t)i_{\alpha ref}(t) + U_\beta(t)i_{\beta ref}(t) \end{aligned}$$

Moreover, the control method performs the step of determining a worst-case active current $i_{aws}(t)$ (block 110), by computing the minimum between the active currents $i_a(t)$ and $i_{aref}(t)$ determined by Equation (12):

$$\text{Equation (13)} \quad i_{aws}(t) = \min(i_a(t), i_{aref}(t))$$

The method further performs the step of determining two maximum absolute correction signals $i_{dmax}(t)$ and $i_{qmax}(t)$ (block 120), using the value $i_{aref}(t)$ computed by Equation (12a) :

$$\begin{aligned} \text{Equation (14)} \quad i_{dmax}(t) &= \frac{i_{aref}(t)U_d(t)}{U_d(t)^2 + U_q(t)^2} \\ i_{qmax}(t) &= \frac{i_{aref}(t)U_q(t)}{U_d(t)^2 + U_q(t)^2} \end{aligned}$$

Applicant has found that maximum absolute correction signals $i_{dmax}(t)$ and

$i_{qmax}(t)$ represent the maximum absolute corrections that yield to a zero the active current $i_{aref}(t)$ when subtracted entirely from the respective currents i_d and i_q . In this respect, the modified active current computed with the modifications yields:

$$\begin{aligned}
 & (i_{dref}(t) - i_{dmax}(t)) U_d(t) + (i_{qref}(t) - i_{qmax}(t)) U_q(t) = \\
 & = i_{dref}(t) U_d(t) + i_{qref}(t) U_q(t) \\
 & \quad - \frac{i_{aref}(t) U_d(t)^2}{U_d(t)^2 + U_q(t)^2} - \frac{i_{aref}(t) U_q(t)^2}{U_d(t)^2 + U_q(t)^2} \\
 & = i_{aref}(t) - i_{aref}(t) \frac{U_d(t)^2 + U_q(t)^2}{U_d(t)^2 + U_q(t)^2} \\
 & = 0
 \end{aligned}$$

Applicant has found that that nullifying the active current $ia(t)$ corresponds to completely stop any regeneration of current. Applicant has found that to avoid overvoltage, it is not necessary to apply the maximum corrections. Only a fraction of
 15 $i_{dmax}(t)$ and $i_{qmax}(t)$ may be conveniently applied, depending on a voltage level and on some user-defined tuning parameters. Indeed, depending on the voltage level, the active current $ia(t)$ can take also small negative values (that is, to regenerate) with bottom limit $-iaIstAbs(t)$, wherein $iaIstAbs(t)$ is an absolute value computed at next step.

20 Furthermore, the method performs the step of determining the instantaneous maximum allowable regeneration current $iaIstAbs(t)$ (block 130) based on the measured voltage level and a prefixed parameter $iaMaxAbs$ corresponding to a maximum absolute active current for regeneration, for example defined by the user:

25 Equation (15) $i_{aIstAbs}(t) = w_V(t) i_{aMaxAbs}$

wherein $w_V(t)$ is a weight coefficient that depends on the voltage $V_{dc}(t)$ and the nominal DC-link voltage V_{dcnom} and on the highvoltage limit V_{high} . For example, weight coefficient $w_V(t)$ may be 1 if voltage $V_{dc}(t)$ is below the nominal DC-link
 30 voltage V_{dcnom} , weight coefficient $w_V(t)$ may be 0 if voltage $V_{dc}(t)$ is above

highvoltage limit V_{high} . The method may decrease the weight coefficient $w_V(t)$ linearly from 1 to 0 as the DC-link capacitor voltage $V_{dc}(t)$ changes in a prefixed range comprised between nominal DC-link voltage V_{dcnom} to high-voltage limit V_{high} .

5 Equation (16)
$$w_V(t) = \text{sat} \left[\frac{V_{high} - V_{dc}(t)}{V_{high} - V_{dcnom}} \right]_0^1$$

Furthermore, the method determines the negative fraction of correction to be applied according, for example, to the empirical saturated-cubic Equation (block 140):

10 Equation (17)
$$\rho(t) = \text{sat} \left[\left(\frac{i_{aws}(t) + i_{aIstAbs}(t)}{i_{aIstAbs}(t)} \right)^3 \right]_{-1}^0$$

15 It is understood that when there is regeneration, the current $i_{aws}(t)$ is negative. Therefore only for active currents $i_a(t)$ below the instantaneous limit $-i_{aIstAbs}(t)$, the fraction $\rho(t)$ counts negative and different from zero.

Furthermore, the method determines the unconstrained d-q axis-wise corrections as a fraction of the maximum correction by the following Equation (block 20 150):

Equation (18)
$$\begin{aligned} i_{dunc}(t) &= \rho(t) i_{dmax}(t) \\ i_{qunc}(t) &= \rho(t) i_{qmax}(t) \end{aligned}$$

25

Furthermore, the method determines the constrained d-q axis-wise current corrections by applying the following saturation and correction Equations (block 160):

Equation (19)
$$i_{q_{corr}}(t) = \begin{cases} \max(i_{q_{unc}}(t), 0), & \text{if } \omega(t) > 0 \\ \min(i_{q_{unc}}(t), 0), & \text{if } \omega(t) < 0 \end{cases}$$

5

Equation (20)
$$i_{d_{corr}}(t) = \min(i_{d_{unc}}(t), 0) - K_{qd} \text{abs}(i_{q_{corr}}(t) - i_{q_{unc}}(t))$$

wherein K_{qd} is a positive tuning gain that may be used to transfer to the d-axis part of the correction originally computed for the q-axis, when saturation occurs.

10 For example, when the motor speed is positive, the method may only permit the q-axis correction to negative and vice-versa.

The method can perform a d-axis correction that is negative and amplified in case the constrained q-axis correction is different from the unconstrained one.

Furthermore, the method may determine the modified current references for
15 the current regulators (block 160) by the adders 30, 31:

Equation (21)
$$\begin{aligned} i_{d_{refMod}}(t) &= i_{d_{ref}}(t) + i_{d_{corr}}(t) \\ i_{q_{refMod}}(t) &= i_{q_{ref}}(t) + i_{q_{corr}}(t) \end{aligned}$$

The advantages resulting from the use of the active voltage limiter unit 15 in
20 the inverter-based apparatus 1 are remarkable.

The active voltage limiter unit has the technical effect of reducing the magnitude of the active current to zero when current starts to become negative, by modifying the current parameters through rotation of the controlled current vector.

Moreover, the capacitor-less inverter-based apparatus is less expensive and
25 less bulky compared to the known inverter-based apparatus. Indeed inverter-based apparatus limits harmonics without usage of dedicated circuitry (PFC), increasing the lifetime expectation of the inverter thanks to, for example, the usage of a film capacitor instead of an electrolytic type. Moreover, capacitor-less inverter-based apparatus reduces EMC emission due to the limited voltage applied during
30 switching.

CLAIMS

1. Inverter-based apparatus (1) configured to control an electric motor (2), the inverter-based apparatus comprising:

an input stage (4), which is connected to mains lines (8) for receiving AC lines currents and AC mains voltage and configured to convert said alternating mains voltage AC to a rectified DC voltage;

an electrolytic-capacitor-less inverter (5), which is configured to generate output currents to be fed to said electric motor (2) based on duty cycles of switching signals;

a DC-link (10), which connects said electrolytic-capacitor-less inverter (5) to said input stage (4) and is crossed by DC-link currents from, or towards, said electrolytic-capacitor-less inverter (5);

a DC-link capacitor (11) connected to said DC-link (10);

a voltage sensor (13) configured to determine the amplitude of said DC-link capacitor voltage ($V_{dc}(t)$);

one or more current sensors (12) configured to determine the amplitude of output currents provided to said electric motor (2) by said electrolytic-capacitor-less inverter (5); and

a current regulator system (14), which is configured to control said duty cycles based on determined current references (i_{dref} , i_{qref}) and said output currents, said inverter-based apparatus (1) being characterized by comprising an active voltage limiter unit (15), which is configured to regulate said current references (i_{dref} , i_{qref}) of said current regulator system (14) in order to limit said DC-link capacitor voltage ($V_{dc}(t)$) within a predetermined voltage range.

2. Inverter-based apparatus according to claim 1, wherein said active voltage limiter unit (15) is further configured to regulate said current references (i_{dref} , i_{qref}) of said current regulator system (14) without using said lines currents and/or DC-link currents.

3. Inverter-based apparatus according to claims 1 or 2, wherein said active voltage limiter unit (15) is further configured to clamp said DC-link capacitor voltage

($V_{dc}(t)$) to a prefixed value, when said electric motor (2) regenerates back current to said the DC-link capacitor (11) via said electrolytic-capacitor-less inverter (5).

4. Inverter-based apparatus according to any of the previous claims, wherein said active voltage limiter unit (15) is further configured to:

5 determine an active current (i_a)(i_{aref}) based on said output currents (i_u , i_v , i_w) and said duty cycles; and

 regulate said current references (i_{dref} , i_{qref}) based on said active current (i_a)(i_{aref}) and said DC-link capacitor voltage ($V_{dc}(t)$) .

5. Inverter-based apparatus according to claim 4, wherein said active voltage
10 limiter unit (15) is further configured to determine a first active current (i_a) based on d-q axis-wise duty cycles (U_d , U_q) which are indicative of said duty cycles of the switching signals and d-q axis-wise currents (i_d , i_q) indicative of said output currents (i_u , i_v , i_w).

6. Inverter-based apparatus according to claims 4 or 5, wherein said active
15 voltage limiter unit (15) is configured to determine a second active current (i_{aref}) based on the d-q axis-wise duty cycles (U_d , U_q) indicative of said duty cycles of the switching signals and said determined current references (i_{dref} , i_{qref}).

7. Inverter-based apparatus according to claims 6 when depending on claim
20 5, wherein said active voltage limiter unit (15) is further configured to determine said active current (i_{aws}) by computing a minimum current between said first ($i_a(t)$) and second active currents ($i_{aref}(t)$).

8. Inverter-based apparatus according to claim 7, wherein said active voltage
25 limiter unit (15) is further configured to determine two maximum absolute correction signals ($i_{dmax}(t)$, $i_{qmax}(t)$) on the basis of said second active current (i_{aref}) and said d-q axis-wise duty cycles (U_d , U_q).

9. Inverter-based apparatus according to claim 8, wherein said active voltage
limiter unit (15) is further configured to determine an instantaneous maximum
allowable regeneration current ($i_{aIstAbs}(t)$) based on a measured voltage level and a
parameter ($i_{aMaxAbs}$) indicative of a maximum absolute active current for
30 regeneration.

10. Inverter-based apparatus according to claim 9, wherein said active voltage limiter unit (15) is further configured to determine an instantaneous maximum allowable regeneration current ($i_{aIstAbs}(t)$) based on the following equation

$$i_{aIstAbs}(t) = w_V(t) i_{aMaxAbs}$$

wherein $w_V(t)$ is a weight coefficient that depends on said DC-link capacitor voltage ($V_{dc}(t)$), on a nominal DC-link voltage (V_{dcnom}), and on a predetermined high-voltage limit (V_{high}).

11. Inverter-based apparatus according to claim 10, wherein said active voltage limiter unit (15) is further configured to determine a negative fraction of correction to be applied according to an empirical saturated-cubic equation:

$$\rho(t) = \text{sat} \left[\left(\frac{i_{a_{ws}}(t) + i_{aIstAbs}(t)}{i_{aIstAbs}(t)} \right)^3 \right]_{-1}^0$$

12. Inverter-based apparatus according to claim 11, wherein said active voltage limiter unit (15) is further configured to determine unconstrained axis-wise corrections as a fraction of the maximum correction by the following equation:

$$\begin{aligned} i_{d_{unc}}(t) &= \rho(t) i_{d_{max}}(t) \\ i_{q_{unc}}(t) &= \rho(t) i_{q_{max}}(t) \end{aligned}$$

13. Inverter-based apparatus according to claim 12, wherein said active voltage limiter unit (15) is further configured to determine constrained axis-wise current corrections by applying the following saturation and correction equations

$$i_{q_{corr}}(t) = \begin{cases} \max(i_{q_{unc}}(t), 0), & \text{if } \omega(t) > 0 \\ \min(i_{q_{unc}}(t), 0), & \text{if } \omega(t) < 0 \end{cases}$$

$$i_{d_{corr}}(t) = \min(i_{d_{unc}}(t), 0) - K_{qd} \text{abs}(i_{q_{corr}}(t) - i_{q_{unc}}(t))$$

wherein:

K_{qd} is a positive tuning gain that may be used to transfer to the d-axis part of the
 5 correction originally computed for the q-axis, when saturation occurs,
 i_{dunc} and i_{qunc} are said axis-wise current corrections .

14. An electric appliance, comprising an electric motor (2) and an inverter-based apparatus (1) according to anyone of claims 1 to 13 to control the electric motor (2).

10 15. Method to control an electric motor by an apparatus comprising an input stage to convert an AC mains voltage to a rectified DC voltage, an electrolytic capacitor-less inverter connected to the input stage by a DC-link, and a capacitor connected to the DC-link, the method comprising the steps of:

- generating, by the electrolytic capacitor-less inverter, output currents to be fed
 15 to the electric motor based on duty cycles of switching signals;
- determining the output currents fed to the electric motor;
- controlling the duty cycles based on current references and the determined output currents;
- determining the voltage across the capacitor; and
- 20 • regulating the current references so as to limit the capacitor voltage within a predetermined voltage range.

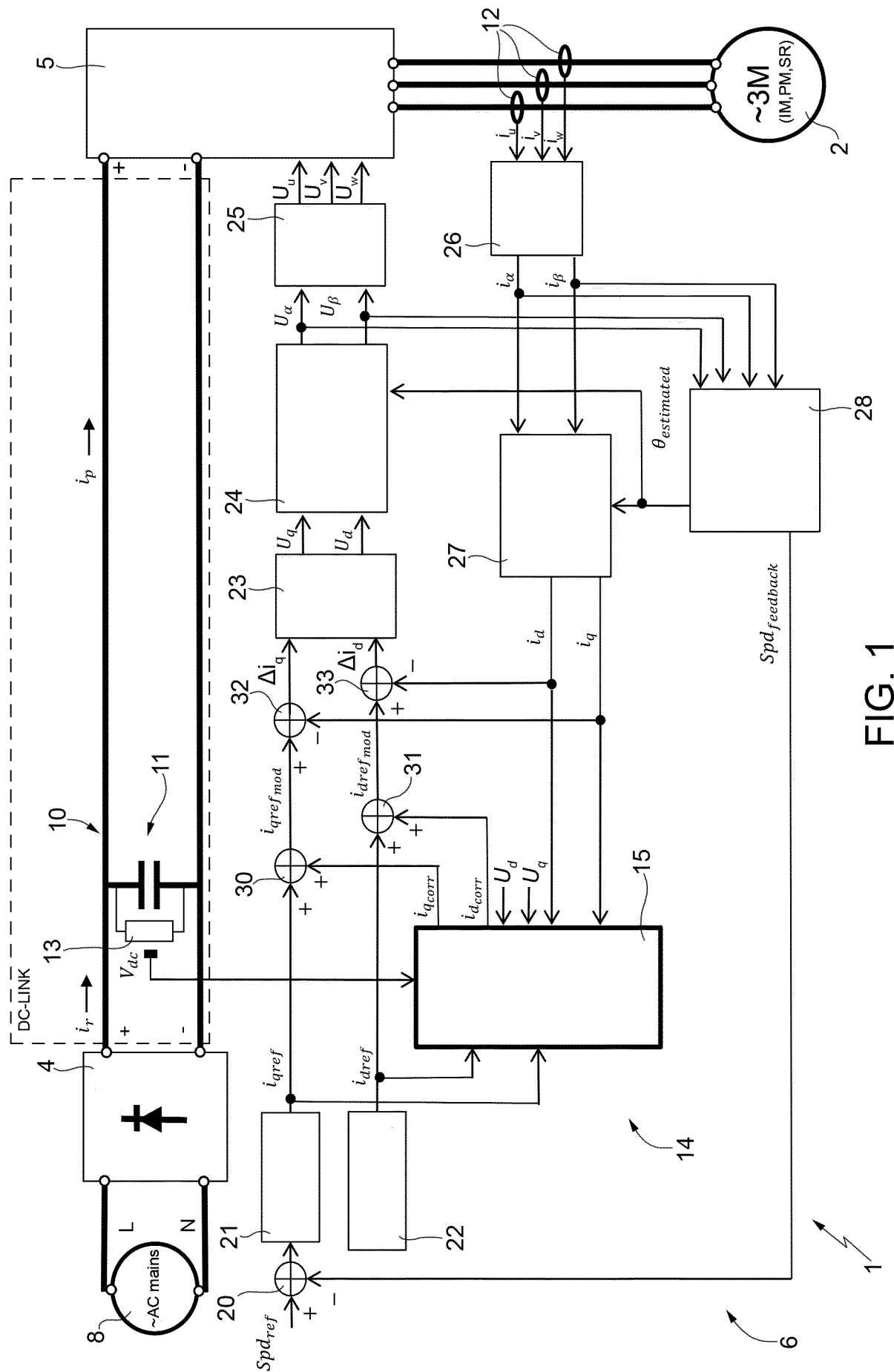


FIG. 1

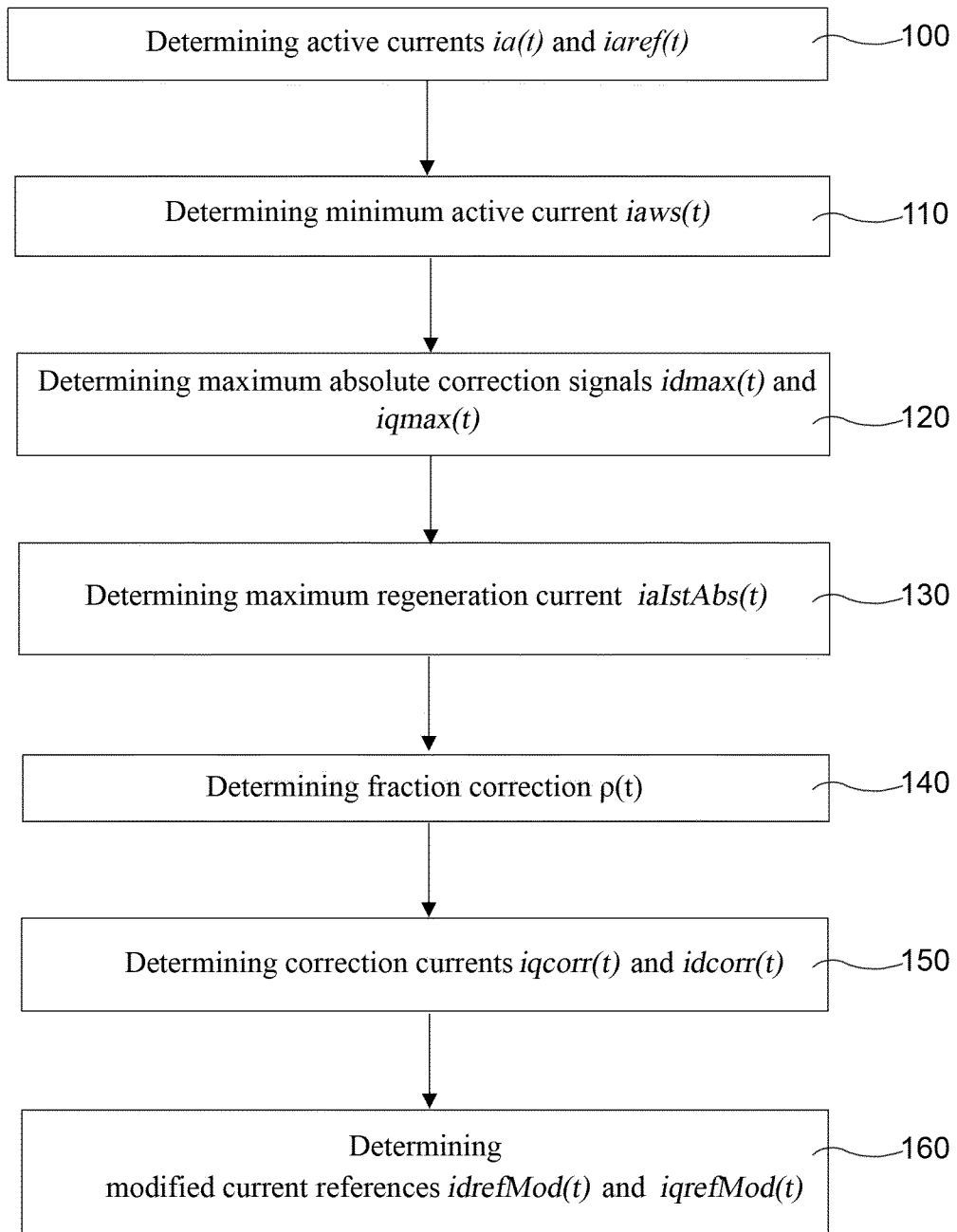


FIG. 2

INTERNATIONAL SEARCH REPORT

International application No
PCT/EP2019/069227

A. CLASSIFICATION OF SUBJECT MATTER

INV. H02M1/32 H02M5/458 H02P3/18
ADD.

According to International Patent Classification (IPC) or to both national classification and IPC

B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)
H02M H02P

Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched

Electronic data base consulted during the international search (name of data base and, where practicable, search terms used)

EPO-Internal, WPI Data

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
X	US 2014/265987 A1 (CHRETIEN LUDOVIC ANDRE [US] ET AL) 18 September 2014 (2014-09-18) the whole document	1-3,14, 15
A	WO 2014/130201 A1 (REGAL BELOIT AMERICA INC [US]) 28 August 2014 (2014-08-28) the whole document	1-15
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☒ Further documents are listed in the continuation of Box C.

☒ See patent family annex.

* Special categories of cited documents :

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Date of the actual completion of the international search

9 October 2019

Date of mailing of the international search report

21/10/2019

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INTERNATIONAL SEARCH REPORT

International application No

PCT/EP2019/069227

C(Continuation). DOCUMENTS CONSIDERED TO BE RELEVANT		
Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	DE OLIVEIRA FILHO M E ET AL: "A control method for voltage source inverter without dc link capacitor", POWER ELECTRONICS SPECIALISTS CONFERENCE, 2008. PESC 2008. IEEE, IEEE, PISCATAWAY, NJ, USA, 15 June 2008 (2008-06-15), pages 4432-4437, XP031300651, ISBN: 978-1-4244-1667-7 page 4435, section B "Protection Circuits"; figures 2,3 abstract -----	1-15

INTERNATIONAL SEARCH REPORT

Information on patent family members

International application No

PCT/EP2019/069227

Patent document cited in search report	Publication date	Patent family member(s)	Publication date
US 2014265987	A1	18-09-2014	NONE

WO 2014130201	A1	28-08-2014	AU 2013204591 A1 07-08-2014
			EP 2949036 A1 02-12-2015
			US 2014203755 A1 24-07-2014
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			WO 2014130201 A1 28-08-2014
