

(10) **Patent No.:** US 8,981,737 B2
(45) **Date of Patent:** Mar. 17, 2015

- (56) **References Cited**

- U.S. PATENT DOCUMENTS

- | | | | | |
|--------------|------|---------|-----------------------|---------|
| 8,350,543 | B2 * | 1/2013 | Loikkanen et al. | 323/259 |
| 2006/0284606 | A1 | 12/2006 | Chen et al. | |
| 2009/0003021 | A1 | 1/2009 | Tsukamoto | |

- FOREIGN PATENT DOCUMENTS

- | | | |
|----|------------|--------|
| CN | 101499717 | 8/2009 |
| JP | 2003011392 | 1/2003 |

- * cited by examiner

- (21) Appl. No.: 13/341,496

- Primary Examiner* — Harry Behm

- (22) Filed: **Dec. 30, 2011**

- Assistant Examiner — Matthew Grubb

- (65) **Prior Publication Data**

- (74) *Attorney, Agent, or Firm* — Paul A. Bernkopf; Bryan A. Santarelli; Lane Powell PC

- US 2012/0229110 A1 Sep. 13, 2012

- (57) **ABSTRACT**

- ### Related U.S. Application Data

- (60) Provisional application No. 61/450,487, filed on Mar. 8, 2011, provisional application No. 61/567,420, filed on Dec. 6, 2011.

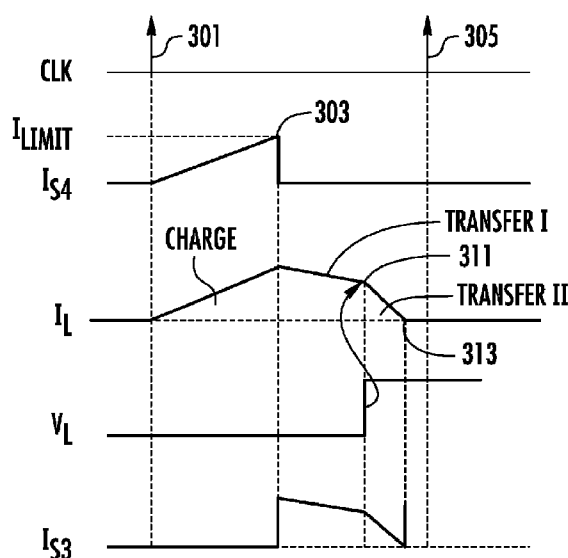
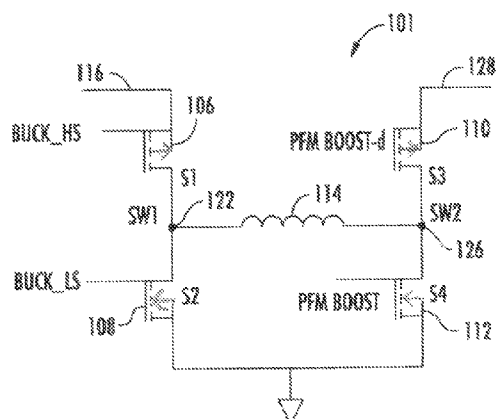
- A buck/boost voltage regulator generates a regulated output voltage responsive to an input voltage and a plurality of control signals. The buck/boost voltage regulator includes a plurality of switching transistors responsive to the plurality of control signals. Control circuitry monitors the regulated output voltage and generates the plurality of control signals responsive thereto. The control circuitry controls the operation of the plurality of switching transistors to enable a charging phase in a first mode of operation, a pass through phase in a second mode of operation and a discharge phase in a third mode of operation within the buck/boost voltage regulator to eliminate occurrence of a four switch switching condition.

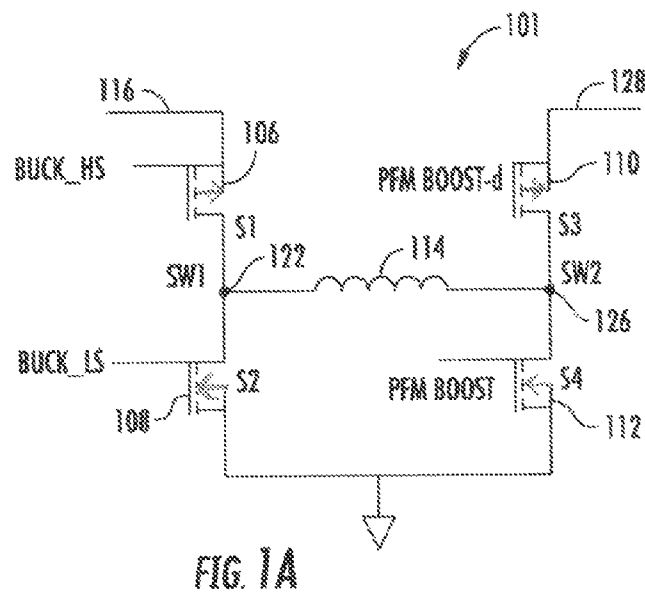
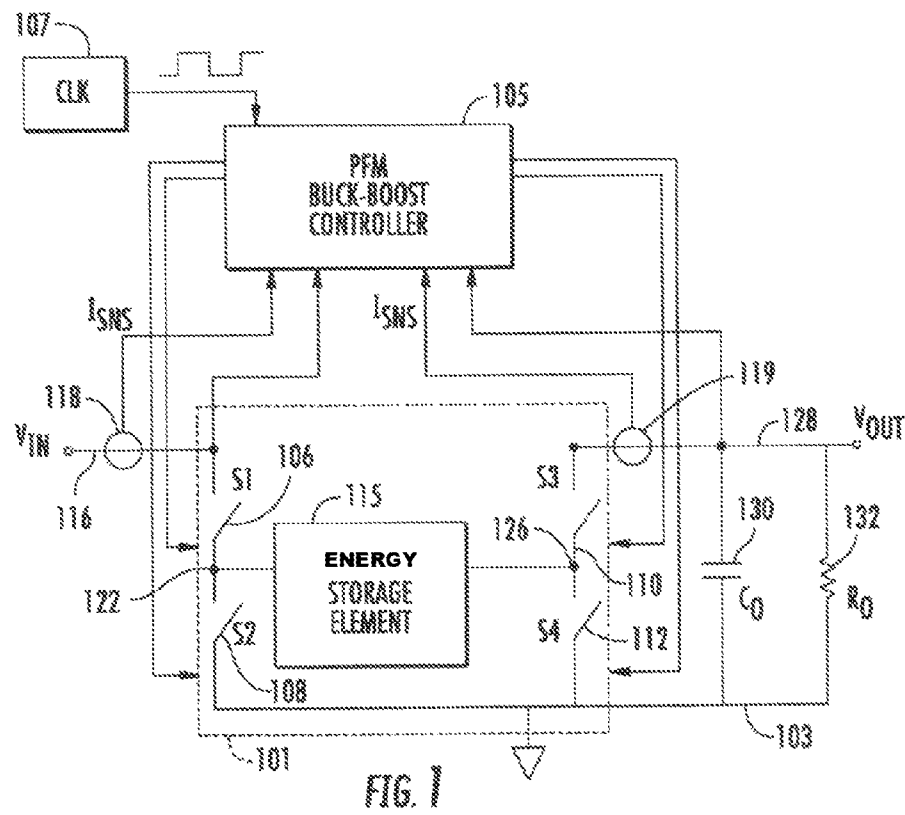
- (51) **Int. Cl.**
H02M 3/158 (2006.01)

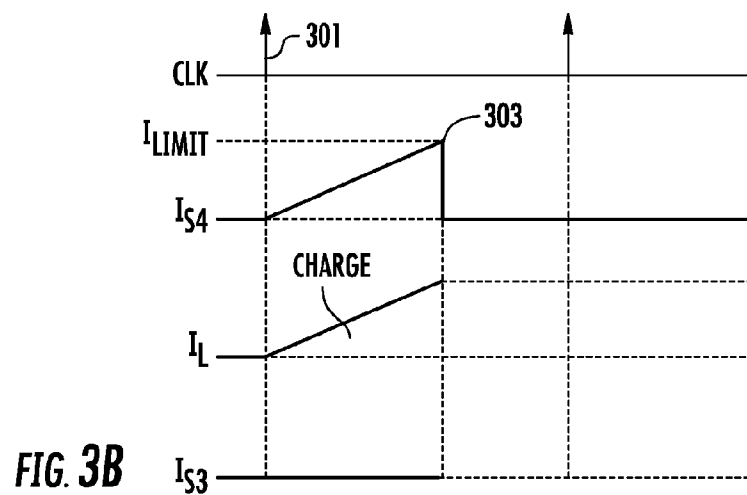
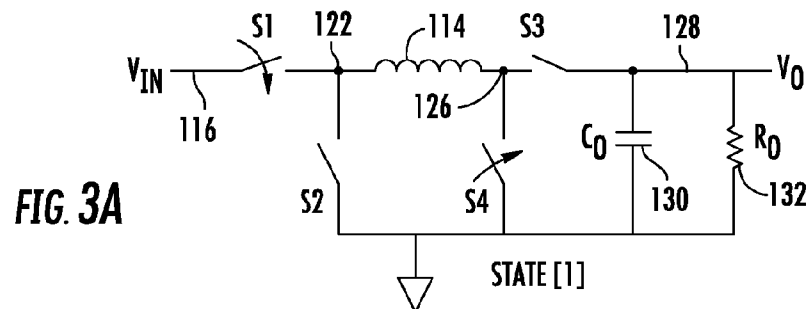
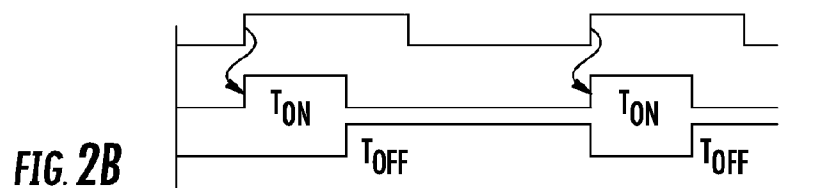
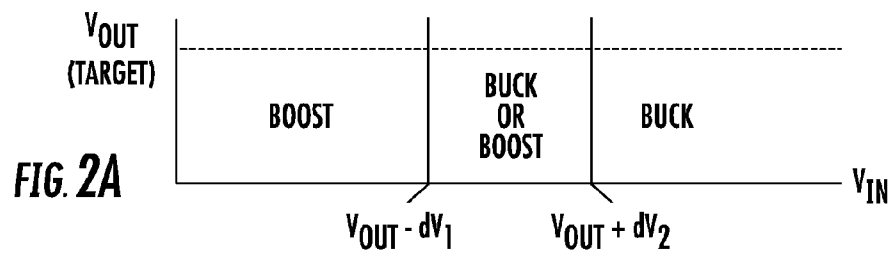
- (52) **U.S. Cl.**
CPC *H02M 3/1582* (2013.01)
USPC **323/259; 323/271**

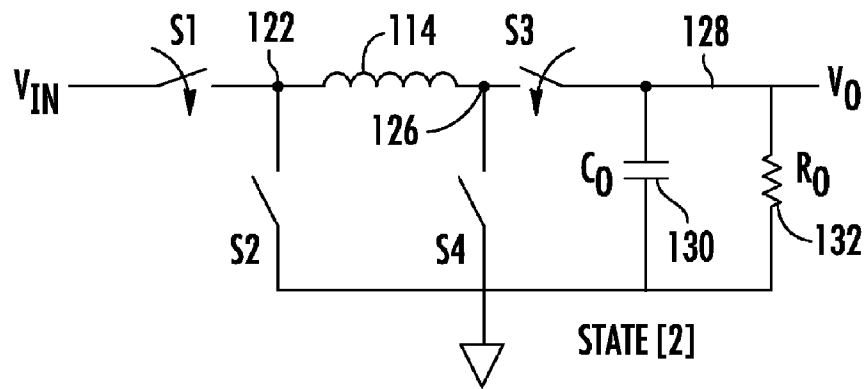
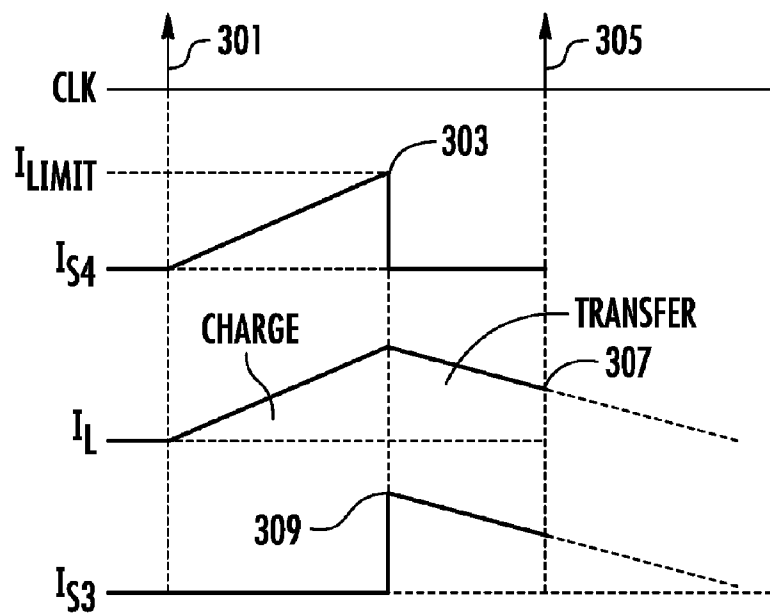
- (58) **Field of Classification Search**
CPC H02M 3/158; H02M 3/1582
USPC 323/259, 271, 225, 344
See application file for complete search history.

- 23 Claims, 13 Drawing Sheets**







**FIG. 4A****FIG. 4B**

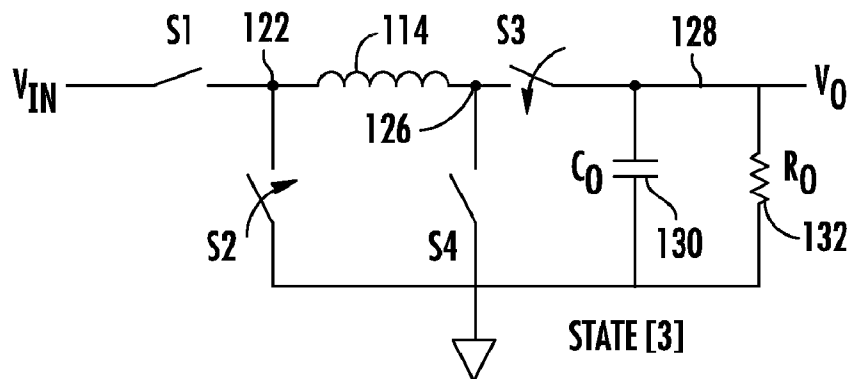


FIG. 5A

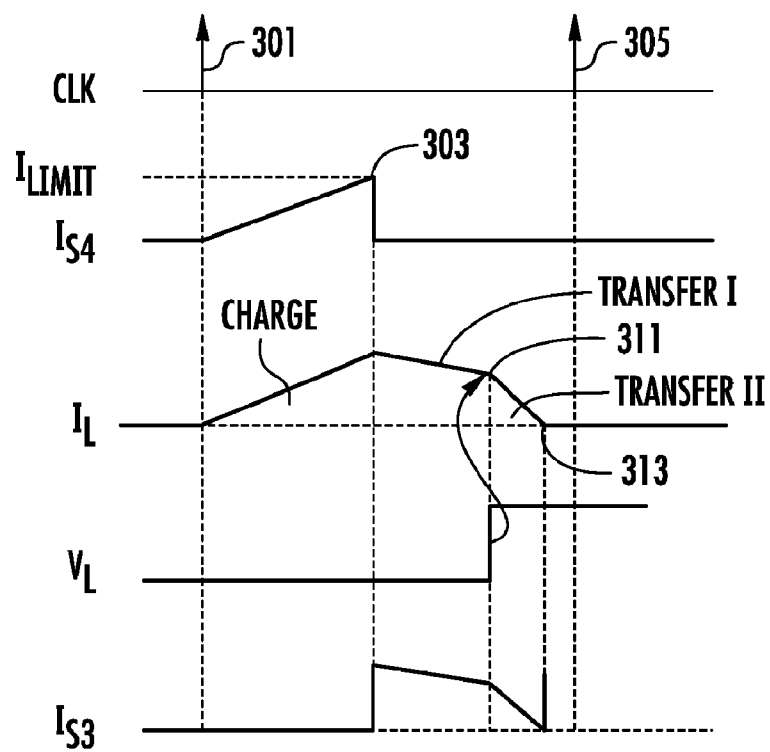


FIG. 5B

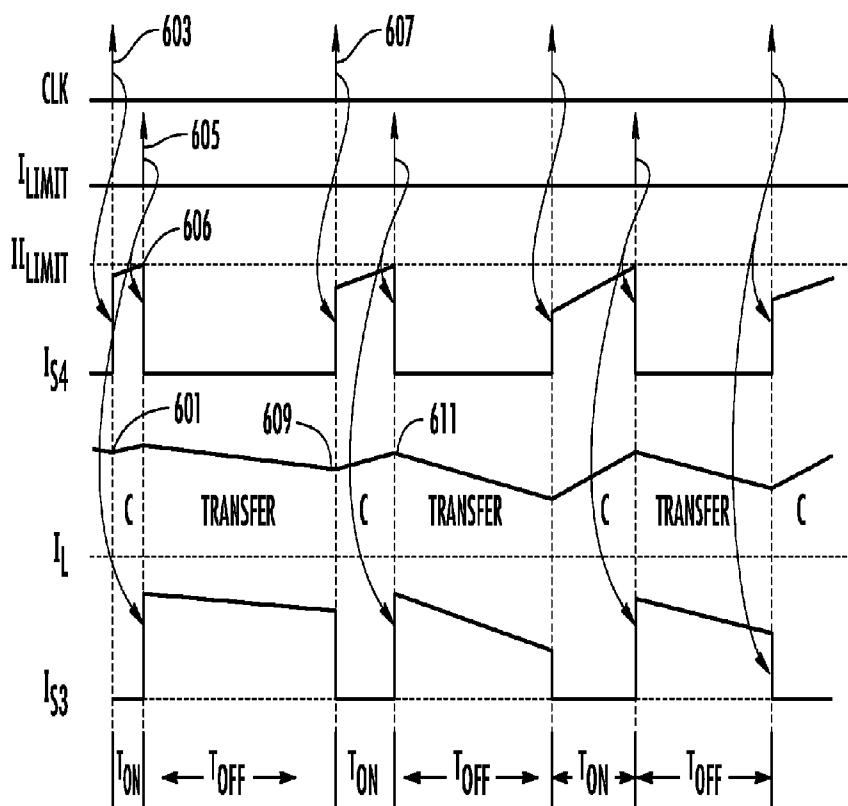


FIG. 6

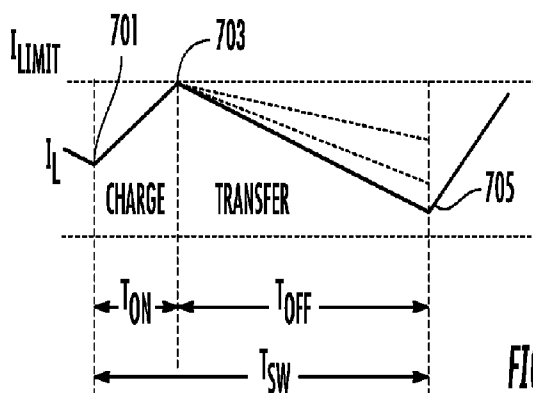
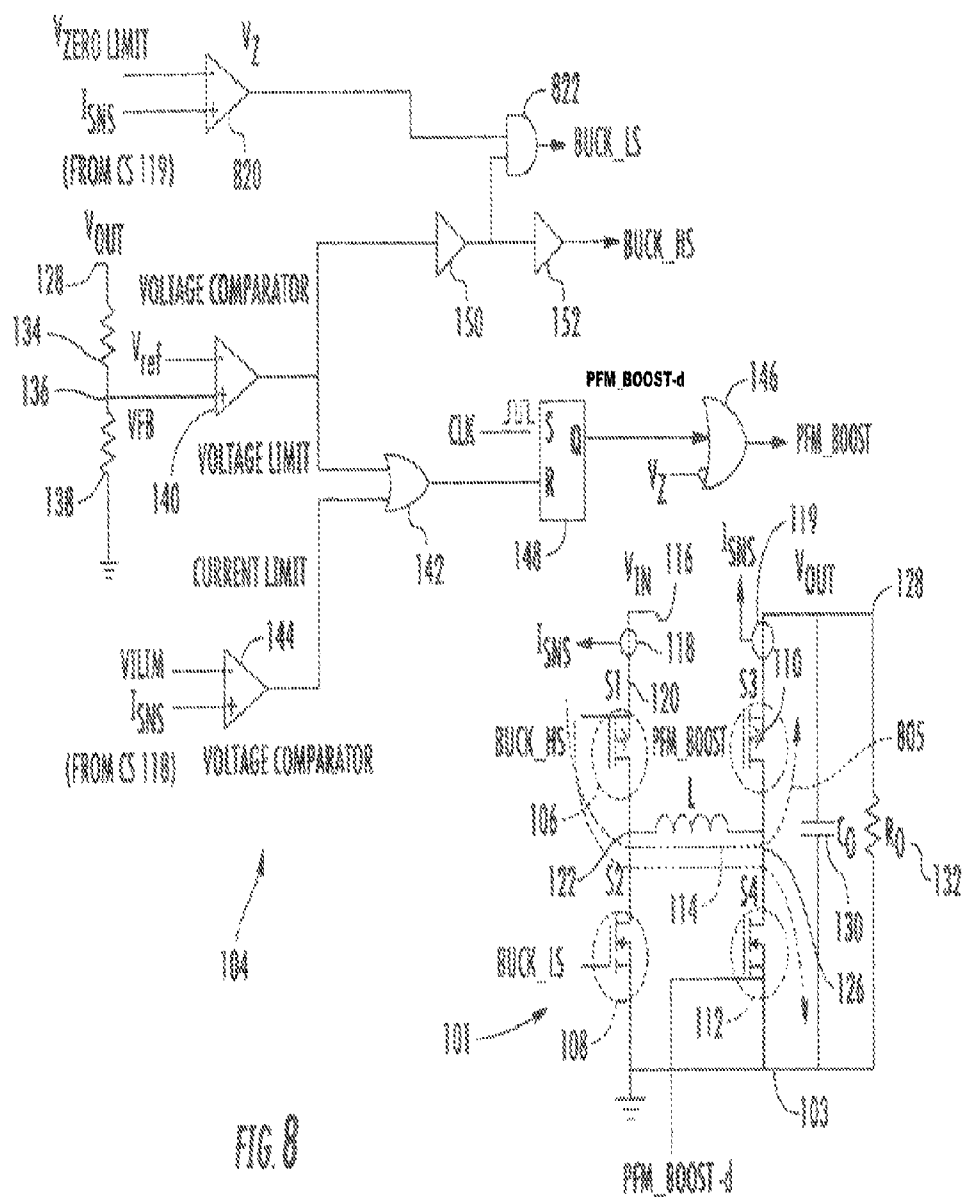


FIG. 7



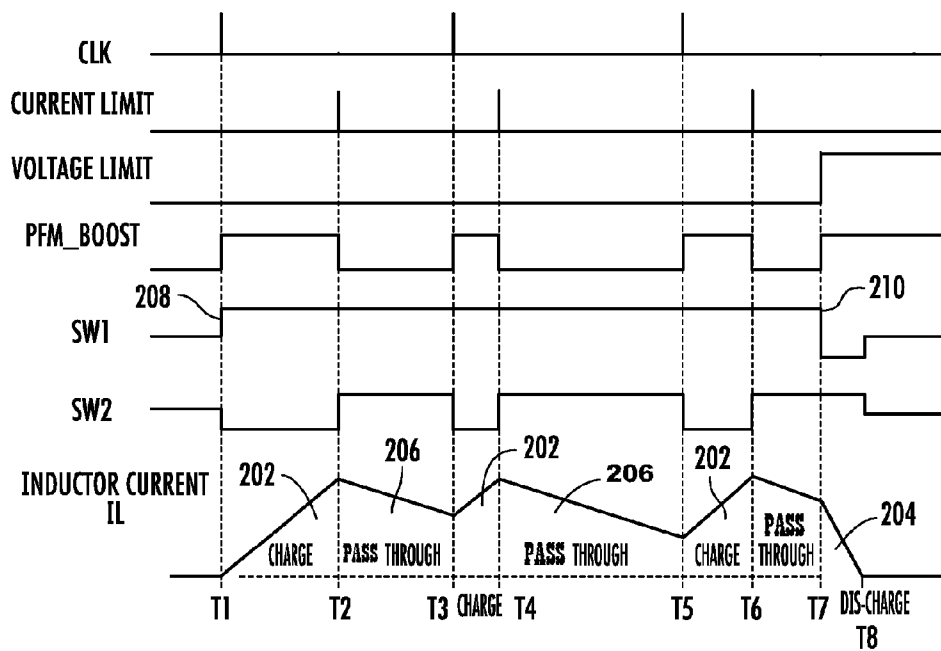


FIG. 9

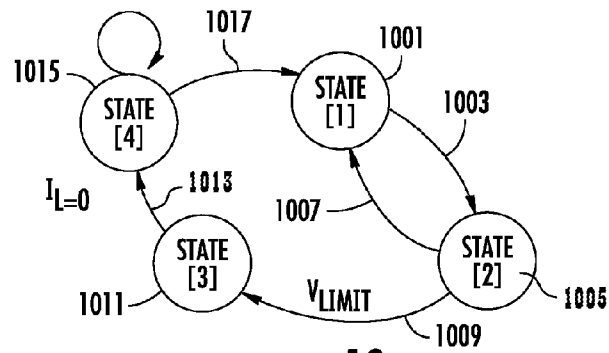


FIG. 10

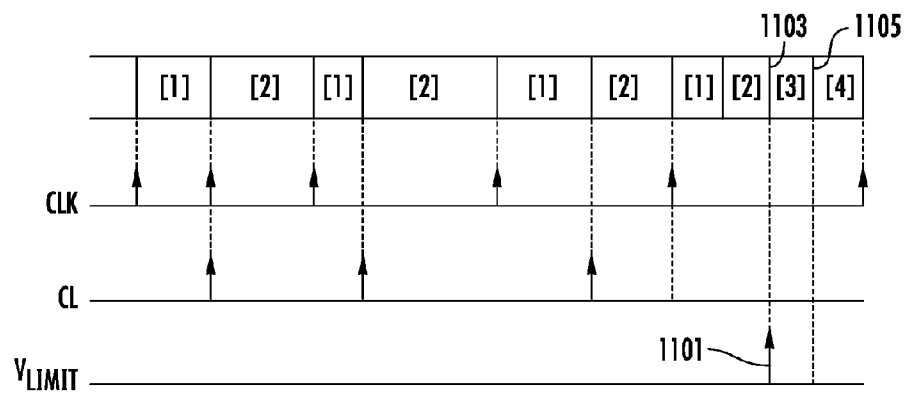
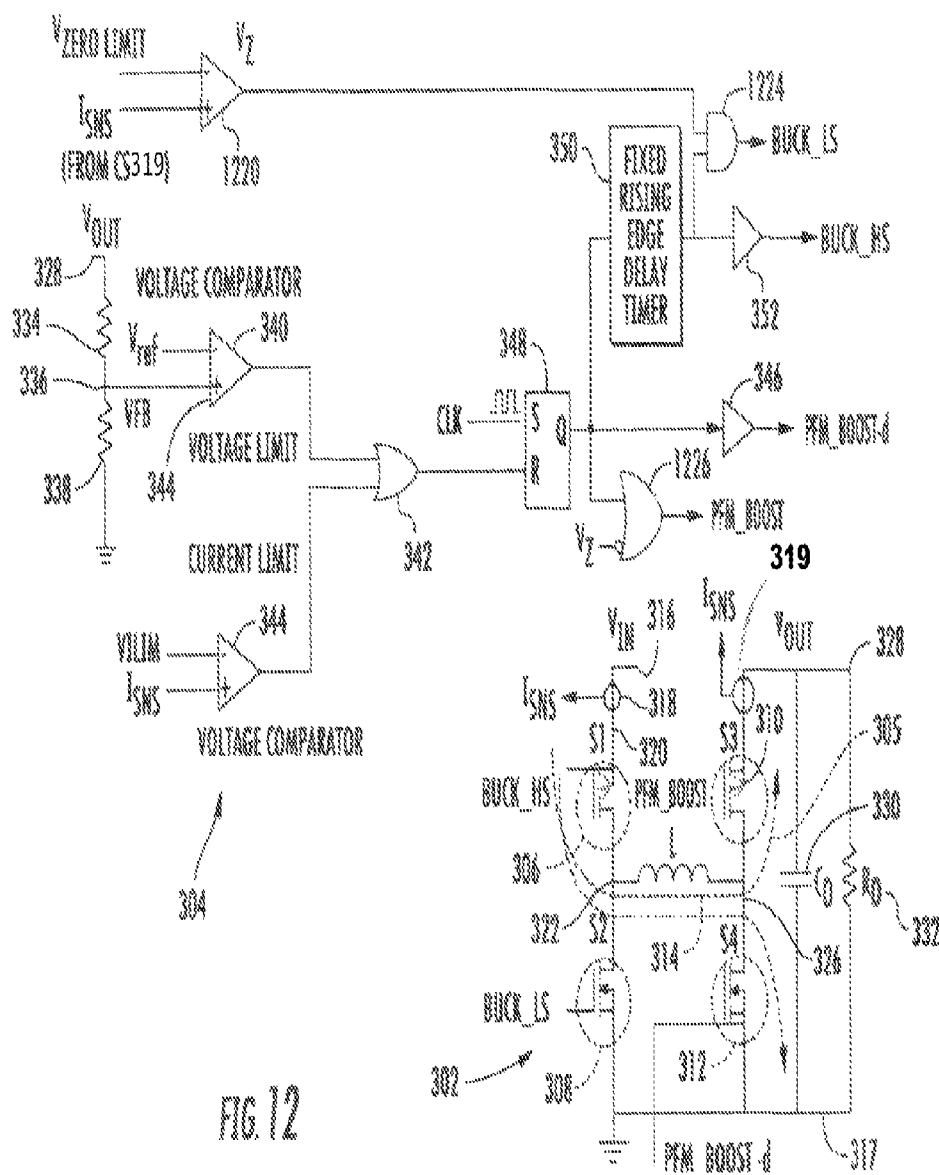
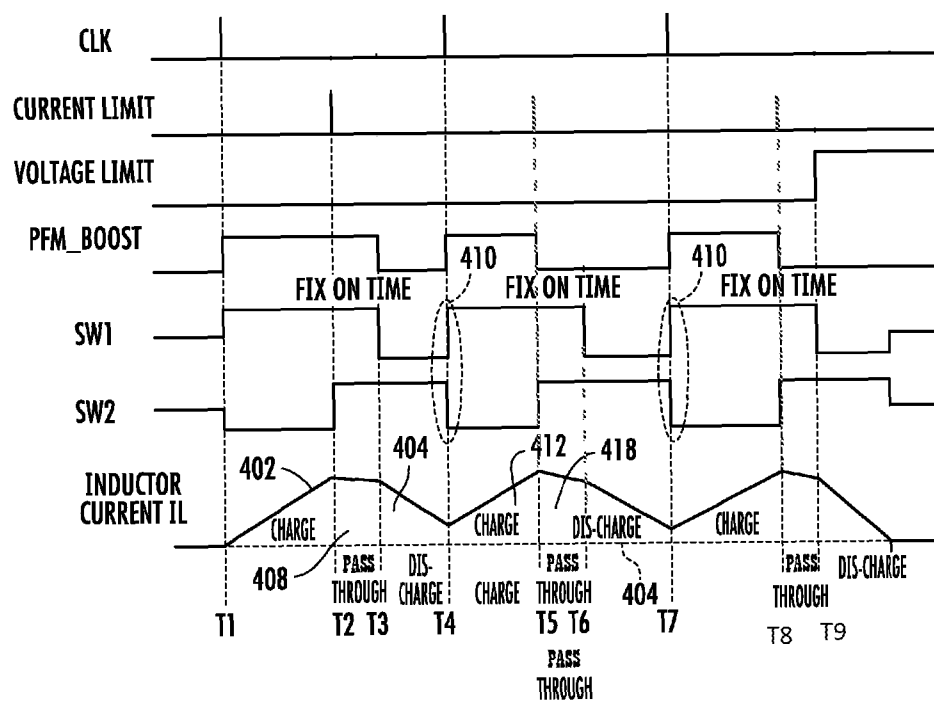


FIG. 11



**FIG. 13**

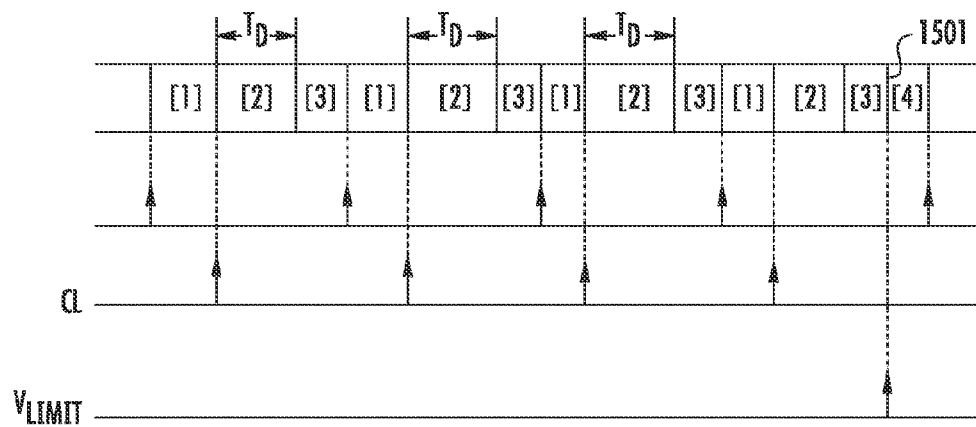
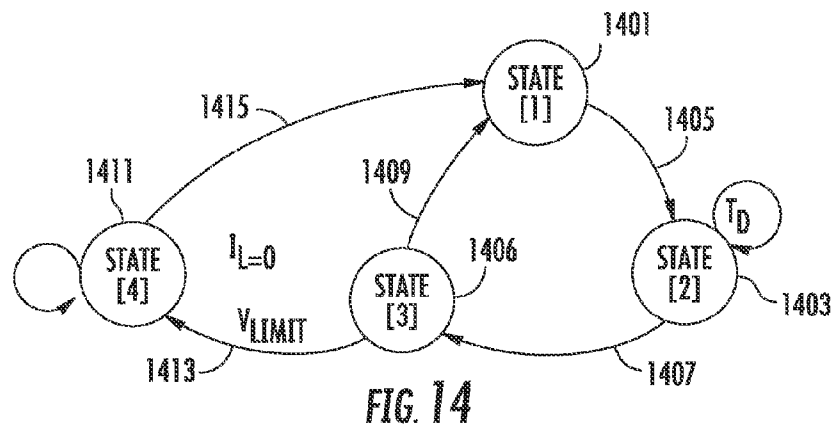


FIG. 15

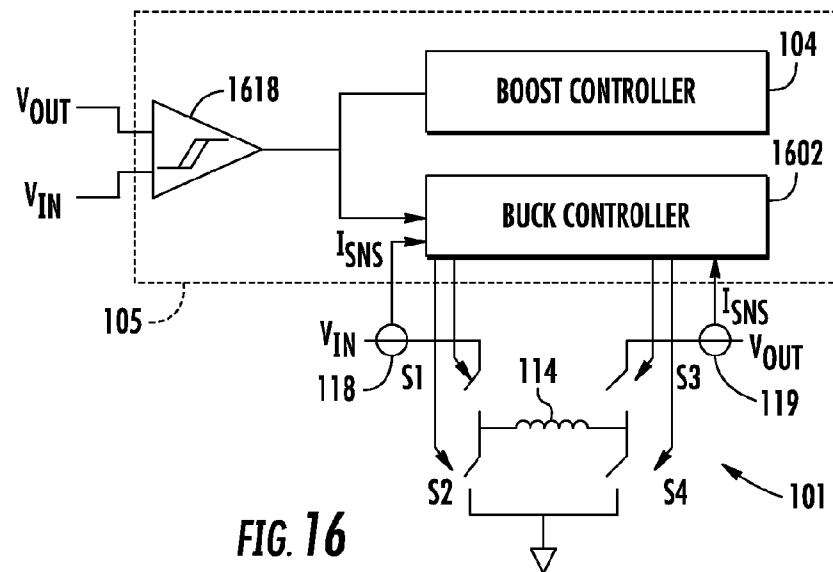


FIG. 16

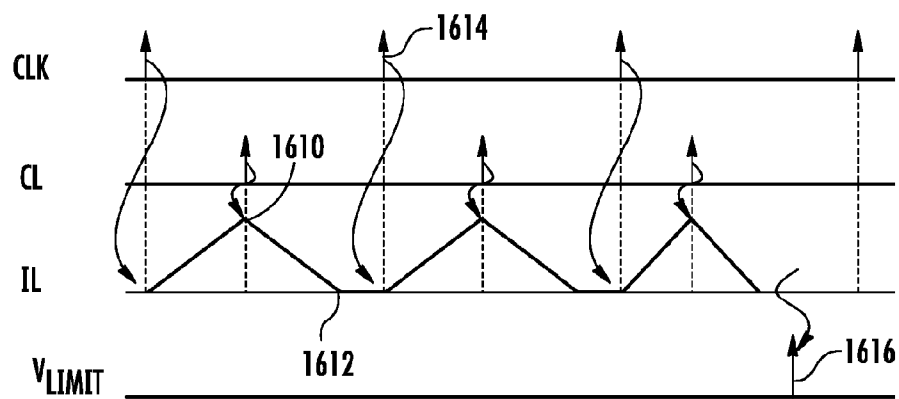


FIG. 16A

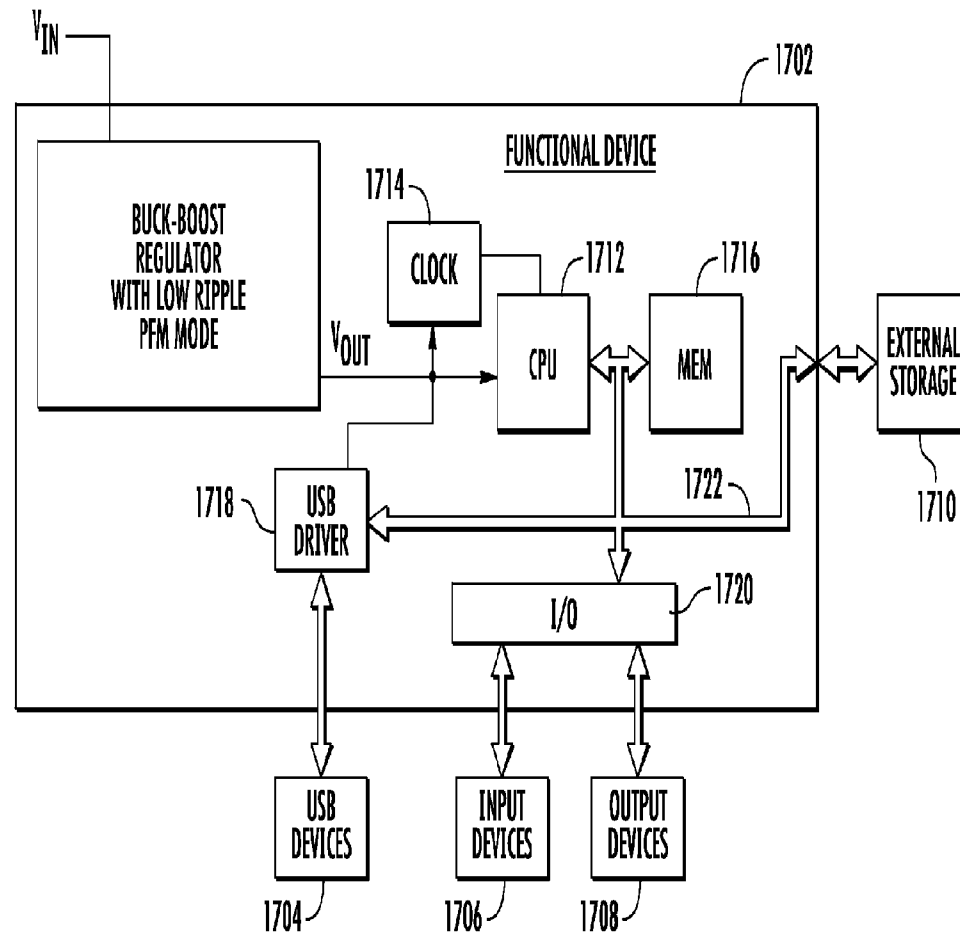


FIG. 17

1

HIGH EFFICIENCY PFM CONTROL FOR BUCK-BOOST CONVERTER

PRIORITY CLAIM

This application claims priority from U.S. Provisional Application No. 61/567,420, filed Dec. 6, 2011, entitled HIGH EFFICIENCY PFM CONTROL FOR BUCK BOOST CONVERTER, and from U.S. Provisional Application No. 61/450,487, filed Mar. 8, 2011, entitled HIGH EFFICIENCY PFM CONTROL FOR BUCK-BOOST CONVERTER, the specification of which is incorporated herein in its entirety.

BRIEF DESCRIPTION OF THE DRAWINGS

For a more complete understanding, reference is now made to the following description taken in conjunction with the accompanying Drawings in which:

FIG. 1 illustrates a top level view of a PFM buck-boost DC/DC converter;

FIG. 1A illustrates a detailed schematic diagram of the H-Bridge switch;

FIG. 2 illustrates a diagrammatic view of the different operational modes of operation for the buck-boost converter as a function of the input voltage;

FIGS. 3A and 3B illustrate one state of the switch operation for the boost mode illustrating the switch states and the associated timing diagrams;

FIGS. 4A and 4B illustrate a second state of the switch operation for the boost mode illustrating the switch states and associated timing diagrams;

FIGS. 5A and 5B illustrate a third state of the switch operation for the boost mode illustrating the switch states and the associated timing diagrams;

FIG. 6 illustrates a timing diagram for boosting the voltage using the first and second states in a PFM operation;

FIG. 7 illustrates the inductor current for a single cycle of the PFM operation of FIG. 6;

FIG. 8 illustrates a first embodiment of the boost operation of the buck-boost converter and associated control circuitry having an improved boost PFM control scheme;

FIG. 9 illustrates the waveforms associated with the operation of the buck-boost converter of FIG. 8;

FIG. 10 illustrates a state diagram of the embodiment of FIGS. 8 and 9;

FIG. 11 illustrates the timing diagram for the state diagram of FIG. 10;

FIG. 12 illustrates an alternative embodiment of the boost operation of the buck-boost converter and associated control circuitry with an improved buck-boost PFM control scheme;

FIG. 13 illustrates the waveforms associated with the operation of the buck-boost converter of FIG. 12;

FIG. 14 illustrates a state diagram for the embodiment of FIGS. 12 and 13;

FIG. 15 illustrates a timing diagram for the state diagram of FIG. 14;

FIGS. 16 and 16A illustrate the operation of the buck side of the converter; and

FIG. 17 illustrates an electronic/electric system including electronic/electric circuitry including the switching circuitry according to one embodiment.

DETAILED DESCRIPTION

Referring now to the drawings, wherein like reference numbers are used herein to designate like elements throughout, the various views and embodiments of a system and

2

method for high efficiency PFM (Pulse Frequency Modulation) control of buck-boost converter are illustrated and described, and other possible embodiments are described. The figures are not necessarily drawn to scale, and in some instances the drawings have been exaggerated and/or simplified in places for illustrative purposes only. One of ordinary skill in the art will appreciate the many possible applications and variations based on the following examples of possible embodiments.

Referring now to FIG. 1, there is illustrated a diagrammatic view at a high level for a Pulse Frequency Modulation (PFM) buck-boost DC/DC converter. The DC/DC converter is comprised of a switching bridge 101 that is operable to transfer charge from a voltage input terminal 116 labeled V_{IN} to transfer charge to an energy storage element 115 and then transfer this charge to a load configured as a parallel capacitor 130 labeled C_O and resistor 132 R_O disposed between a voltage output terminal 122 labeled V_{OUT} and a reference voltage on a node 103, which reference voltage is typically disposed at ground. The bridge 101 is controlled by a PFM buck-boost controller 105 which operates in accordance with a Pulse Frequency Modulation (PFM) mode of operation. This PFM operation is divided into two operations, one for charging the energy storage element 115 and one for transferring the energy stored therein to the load. The PFM operation varies the ratio between these two operations, as will be described hereinbelow. A clock input from a clock 107 provides the time base for the PFM operation.

The bridge 101 is an H-bridge. This is comprised of two nodes 122 and 126 with an energy storage element 115 disposed therebetween. A first switch 106 is connected between the input node 116 and a node 122. A second switch 108 is connected between a node 106 and reference node 103. These two switches 106 and 108, as will be described hereinbelow, are typically used for the buck side of a buck-boost converter. The other side of the H-bridge is comprised of a first switch 110 connected between the output voltage terminal 128 and the node 126 on the other side of the energy storage element 115, and a second switch 112 is connected between node 122 and the reference node 103. The switches 110 and 112 are typically used for the boost portion of a buck-boost converter. However, the H-bridge configuration allows versatility in how the charge is transferred to the energy storage element 115 and then from the energy storage element 115 to the output terminal 128, as will be described in more detail hereinbelow.

Referring now to FIG. 1A, there is illustrated a more detailed diagrammatic view of the implementation of the H-bridge 101. In this configuration, the switch 106 is configured with a p-channel transistor, switch 108 is configured with an n-channel transistor, switch 110 is configured with a p-channel transistor and a switch 112 is configured with an n-channel transistor. The signals that control the gates of transistors 106 and 108 are the BUCK_HS and BUCK_LS signals, respectively. Similarly, the signals that control the gates of transistors 110 and 112 are PFM Boost-d and PFM Boost, respectively. The term "switch" for the elements 106, 108, 110 and 112 will be interchangeable with the term "transistor" for the same elements throughout this Specification. The energy storage element 115 is comprised of an inductor 114 connected between the nodes 122 and 126.

Referring now to FIG. 2A, there is illustrated a plot of input voltage as a function of the buck-boost mode relating to a target V_{OUT} voltage. This V_{OUT} voltage is illustrated by a dashed line. When the input voltage is less than $V_{OUT-TARGET} - dV_1$, the DC/DC converter operates in the boost mode. When V_{IN} is between the voltage $V_{OUT-TARGET} +$

3

dV_2 , and $V_{OUT-TARGET}-dV_1$, the DC/DC converter operates in either the buck or boost mode. If V_{IN} is greater than $V_{OUT-TARGET}+dV_2$, the DC/DC converter operates in the buck mode. When operating in the buck-boost mode, this is typically referred to as a "transition" phase.

The DC/DC converter operates utilizing Pulse Frequency Modulation (PFM), which is sometimes referred to as the Pulse Frequency Mode. This utilizes a fixed clock frequency wherein the energy storage element 115, e.g., inductor 114, is charged up for a time duration T_{ON} followed by a transfer operation for a time duration T_{OFF} . By varying the ratio between T_{ON} and T_{OFF} , the amount of energy transferred to the load can vary as illustrated in FIG. 2B. In the boost mode, for example, transistor 106 is closed and transistors 110 and 112 are switched for store and transfer operations, as will be described in more detail hereinbelow. To charge the inductor in the boost mode, i.e., to store energy therein, the node 126 is pulled to ground by closing transistor 112 and opening transistor 110 with transistor 106 closed. This is the phase labeled T_{ON} in FIG. 2B. At the end of the T_{ON} period, transistor 112 is opened and transistor 110 is closed, transferring energy to the output terminal 128, this being labeled the T_{OFF} period which extends to the next occurring edge of the clock. By varying the ratio of the duration of these two T_{ON} and T_{OFF} periods, the amount of charge transferred to the load can be varied. This is described in more detail hereinbelow with respect to the operation of the controller 105 in the boost mode.

The operation of the boost mode will be described in the following figures. In general, there will be three states that are present in the boost mode of the disclosed embodiment. There will be a first charge phase to store energy in the inductor 114 followed by a second transfer state which partially transfers energy from the inductor 114 to the load 332 and a third transfer state that fully transfers the energy in the inductor 114 to the load.

Referring to FIG. 3A, there is illustrated a diagrammatic view of the switches illustrated in a simplified diagrammatic view. For simplicity purposes, transistor 106 is labeled S1, transistor 108 is labeled S2, transistor 110 is labeled S3 and transistor 112 is labeled S4, with only the designations S1, S2, S3 and S4 illustrated. In the first state, labeled STATE [1], the charge operation is illustrated. In this operation, S1 is closed and S2 is opened such that the voltage V_{IN} of terminal 116 is connected to node 122, and node 122 is connected to one side of the inductor 114. The other side of the inductor 114 is connected to node 126, which node 126 is connected to the reference voltage via a switch S4, with switch S3 opened. This will allow the inductor current to ramp up. FIG. 3B illustrates this operation. The switch configuration of FIG. 3A in the first state is initiated at a clock edge 301. The current through the switch S4 is illustrated with the waveform I_{S4} illustrating the current ramping up to a point 303 at a current limit. This is a predetermined current value to which the current stored in the inductor 114 can ramp to. Once the current is detected as being at that level, switch S4 will be opened at point 303, which is the time of the peak of the current in the inductor 114, which is illustrated in FIG. 3B as the waveform labeled I_L to end the charge operation.

Referring now to FIGS. 4A and 4B, there is illustrated a simplified diagrammatic view of the switches in STATE [2] and the associated timing diagram. When the inductor current has reached the predetermined current limit, as described hereinabove, the state is switched from STATE [1] to STATE [2], wherein switch S4 is opened and switch S3 is closed at point 303. This results in node 126 being connected to the output terminal 128 and to resistor 132. This type of operation is sometimes referred to as the "ringing inductor" operation

4

wherein the voltage across the inductor 114 is reversed, since the current therethrough cannot change instantaneously. Therefore, the voltage on the side of the inductor connected to node 126 will be higher than the voltage on the node 122. This will cause current to flow to node 128 when connected thereto, thus raising its voltage. This will cause a charge transfer to occur until the end of the clock period at the next clock edge 305. This operation between the time at point 303 and the clock edge 305 will result in a decrease in the inductor current I_L indicating a transfer of energy to the load. However, the operation is such that only a partial amount of the energy stored in the inductor will be transferred and, therefore, the inductor current will not be reduced to a zero current level. This is indicated at point 307. Similarly, it can be seen that the current through switch S3 will initially rise to the peak current level at which the inductor current is disposed at a point 309 when closed to indicate current flowing therethrough to node 128. The current through switch S3 is a combination of current from the inductor 114 and current sourced from V_{IN} . This current will track the inductor current to the point 307, at which time the PFM cycle will change to the next State. The current at this point 307 is not at a zero level.

In this STATE [2], the voltage V_{IN} is connected to the load through the inductor 114. Thus, current will flow from the inductor 114 (stored energy) and also from the node 122 sourced by V_{IN} . When V_{IN} is approximately equal to V_{OUT} , the voltage across the inductor 114 will be approximately zero, but current will still flow from V_{IN} .

Referring now to FIGS. 5A and 5B, there is illustrated the third state, STATE [3], for both a simplified diagrammatic view of the switch and an associated timing diagram. In this state, the transfer operation of STATE [2] will be prematurely terminated at a point 311 prior to the occurrence of the next occurring clock edge 305. The state illustrated in FIG. 5A begins at point 311. At this point, an event is detected, such as reaching the voltage limit, i.e., the target voltage. This will result in switch S1 opening and switch S2 closing. When this occurs, the rate of transfer of energy from the inductor 114 to the node 128 will increase, thus increasing the rate of transfer of energy to the load and the rate of current I_L from the inductor 114. This is due in part because no additional current is sourced from V_{IN} . When the current I_L reaches a value of zero, at a point 313, as determined by current sensor 119, the switch S2 and the switch S3 will be opened, as this indicates the DC/DC converter is at the target voltage and no further energy needs to be transferred to the output load. This can be seen with respect to the current through S3, which goes from the peak current through the inductor down to a zero current.

Referring now to FIG. 6, there is illustrated a timing diagram for the operation in one embodiment where STATE [1] and STATE [2] are sequentially sequenced through. The STATE [1] is the charge cycle and is represented by T_{ON} indicating that S1 is closed and S4 is closed and STATE [2] is illustrated by T_{OFF} representing S1 on, S4 off and S3 on. In this illustration, the current in the inductor 114 has never been fully discharged (i.e., has not gone to zero) at the beginning of the operation. The prior occurring state was described with respect to the timing diagram of FIG. 4B wherein, at point 307, the inductor 114 has not been fully discharged and, as such, when the clock edge 305 occurs, energy is left in the inductor 114. This results in a current level at the initiation of the next charge cycle or the beginning of the next STATE. Thus, at a point 601, the current at the end of the previous STATE [2] will be at a level greater than zero. At this point, at a clock edge 603, switch S1 is closed and switch S3 is opened and the current through switch S4 at the clock edge 603 is already high but it is not at the peak level, the level of I_{LIMIT} .

5

the predetermined current limit for the inductor **114**. Thus, additional charge will be transferred to the inductor **114** during this STATE. When the current through the inductor **114** reaches I_{LIMIT} , switch **S3** will close and switch **S4** will open. The current level of I_{LIMIT} is set at a sufficiently high level to ensure there will be enough energy stored in inductor **114** for expected load levels. Thus, when the current level is reached, at a current limit edge **605**, the current through the inductor **114** and through switch **S1** will reach I_{LIMIT} at a point **606** and, when switch **S4** opens, this will be the current level through switch **S3** initially in STATE [2]. Current will be transferred to the load and energy will be depleted from the inductor **112** and, since the side of the inductor **114** on the node **126** connected to the load has a voltage that is initially higher than the input voltage, the voltage on the load will rise above V_{IN} and energy will be transferred thereto, thus decreasing energy in the inductor and decreasing the current through the inductor. This transfer operation of energy from the inductor **114** to the load will occur until the next clock edge, clock edge **607**. At clock edge **607**, switch **S4** is closed and switch **S3** is opened for the next PFM cycle initiated with STATE [1].

Depending upon the load value and the current transferred to the load, the amount of energy removed from the inductor **114** will cause the slope of current depletion from the inductor **114** to be greater or lesser, this being a function of both the value of the load and the voltage between V_{IN} and V_{ON} . Thus, at the next clock cycle **607**, the current level may be lower than at point **601**. In this illustration, at a point **609** on the inductor current waveform, the level of the inductor current at point **609** is lower than the current at point **601**. This will result in the inductor **114** requiring additional time to charge back up to the current I_{LIMIT} at a point **611** which increases the time T_{ON} . Since the time T_{ON} increases, the time T_{OFF} must decrease such that less time is allowed for transfer of energy from the inductor to the load. Thus, since the period of the clock is fixed, the amount of time between T_{ON} and T_{OFF} will dynamically vary. It should be understood that, since this is a boost operation and that node **122** is connected to V_{IN} through the switch **S1** during the transfer state during STATE [1], current is transferred from both the inductor **114** and from V_{IN} . Thus, when the voltage V_{IN} and V_{OUT} are substantially equal at the transition reached between boost and buck operations, the decrease in current from the beginning to the end of T_{OFF} will be very little. This is illustrated in FIG. 7.

With respect to FIG. 7, there is illustrated one cycle of the clock between a point **701** where switch **S4** is closed at an initial current in the previous STATE. Depending on the level of the current, the duration of time T_{ON} will change until the current reaches I_{LIMIT} at a point **703**. This will initiate the next state, STATE [2], for the transfer operation. The length of this time relative to T_{ON} depends upon the level of current at point **701**. The lower the current level, the longer the duration of T_{ON} and the lesser the duration of T_{OFF} . During T_{OFF} , the transfer rate is a function of the load and the voltages between V_{IN} and V_{OUT} . Thus, it can be seen that the slope of the transfer, i.e., the rate at which energy is transferred from the inductor, is depicted with dotted lines illustrating that the slope could be flat, if the voltages are substantially equal, to a steep slope. However, it can be seen that the inductor current does not fall to the zero crossing and only a portion of the energy in the inductor **114** is transferred from the inductor **114** such that, at the beginning of the next STATE [1], at a point **705**, the current through the inductor **114** is not zero. It can be seen that, by not allowing the current through the inductor **114** to go to zero, or to go below (cross) zero, there will be no requirement to open switch **S1** to prevent current from flowing from the load to the inductor **114**, and thus there

6

will be less output ripple and less switching, since switch **S2** has not closed to fully transfer the charge as per STATE [3] described above. As described hereinbelow with respect to FIGS. **5A** and **5B**, at some point during T_{OFF} , switch **S2** is closed and switch **S1** is opened to increase the rate at which energy is discharged from the inductor, since current is no longer being supplied by V_{IN} and, once fully discharged at the zero crossing, all switches **S1**, **S2**, **S3** and **S4** are opened to tri-state nodes **122** and **126**.

With further reference to FIG. 7, it can be seen that the fixed clock will provide a clock period of T_{SW} between clock edges. The peak current level and T_{SW} are selected such that, for all load levels and voltage levels of V_{IN} , V_{OUT} and $V_{OUT-TARGET}$ (or V_{LIMIT}), the current I_L will not fall to a zero current level. Thus, rather than have a fixed T_{ON} , T_{ON} varies and the ratio of T_{ON}/T_{OFF} varies to continually transfer charge during T_{OFF} without the requirement to terminate connection of the inductor to the load until the target voltage is met. This is with respect to a switching operation where switch **S3** is a make or break switch as opposed to a diode that will reverse bias at close to zero current.

Referring now to FIG. 8, there is illustrated a detail of the boost operation of the buck-boost converter, illustrating an H-Bridge **102** and associated boost control circuitry **104** associated with a first embodiment of a boost PFM (Pulse Frequency Modulation) control scheme that utilizes a pass through phase of STATE [2] between the charge and discharge phases of STATE [1] and STATE [3] in order to avoid a four switch switching condition during the boost operation. A four switch switching condition occurs when each of the four switching transistors within a buck-boost converter are switching between one of a logical high or a logical low state at a same period in time. This occurs at the transition of the buck-boost converter from the charge phase to the discharge phase or from the discharge phase to the charge phase if only STATE [1] and STATE [3] were used. The charge phase occurs when the inductor current through the inductor **114** of the buck-boost converter is increasing, and the discharge phase occurs when the inductor current through the buck-boost converter is decreasing towards a zero crossing level. By introducing a transfer operation in a "pass through" phase during boost PFM operation between STATE [1] and STATE [3], the PFM boost mode of operation utilizes a charge phase in STATE [1] followed by a pass through phase in STATE [2] to partially transfer the energy stored in the inductor **114** to the load and then including a discharge phase in STATE [3] at some time within the charging operation to fully discharge the inductor **114**. The pass through phase operation connects V_{IN} to node **122** and node **126** to the output node **128** by turning on transistors **106** and **110** and enables the inductor current I_L to flow from V_{IN} to V_{OUT} as illustrated generally at **805** as well as flow of current from inductor **114**. When the pass through phase is present, there is no point in time at which a four switch switching condition occurs. This improves the efficiency of the buck-boost converter by up to 15% in the boost PFM mode of operation.

Referring now to the drawings, and more particularly to FIG. 8, there is illustrated the H-Bridge **102** and associated control circuitry **104** for a buck-boost converter operating according to an embodiment in the boost mode. The control circuitry **104** monitors the output voltage at node **128** using a resistor divider consisting of a resistor **134** connected between node **128** and node **136** and a resistor **138** connected between node **136** and ground. Node **136** provides the feedback voltage V_{FB} to a non-inverting input of a voltage comparator **140**. The non-inverting input of the voltage comparator **140** receives a reference voltage V_{REF} . The output of the

voltage comparator **140** generates a voltage limit signal that is provided to a first input of an OR gate **142**.

The other input of OR gate **142** is connected to receive a current limit signal from the output of a voltage comparator **144**. The voltage comparator **144** receives the I_{SNS} voltage signal from the current sensor **118** at its non-inverting input and the V_{LIMIT} voltage limit signal at its inverting input. The output of the OR gate **142** is connected to the R input of SR latch **148**. The SR latch **148** is reset dominant to prevent the clock signal CLK from setting the latch if its reset R input is logic “high”, implementing pulse skipping, a form of PFM control. The output of OR gate **142** will generate a logical “high” value responsive to either the voltage limit signal or the current limit signal from the output of comparators **140** and **144**, respectively, going to a logical “high” level. The voltage limit signal goes to a logical “high” level when the feedback voltage V_{FB} exceeds the reference voltage V_{REF} . The current limit signal goes to a logical “high” level when the I_{SNS} signal from the current sensor **118** exceeds the V_{LIMIT} voltage.

The output of comparator **140** is also provided as an input to a buffer **150**. The output of the buffer **150** is connected to one input of an AND gate **822** and provides the BUCK_LS signal which is provided as a control signal to the gate of transistor **108**. The output of buffer **150** is connected to the input of a buffer **152** which provides the BUCK_HS signal at its output. The BUCK_HS signal is applied as a control signal to the gate of transistor **106**.

The SR latch **148**, in addition to receiving the output of the OR gate **142** at its R input receives a clock signal (CLK) at its S input. Responsive to the CLK signal and the output of the OR gate **142**, the SR latch **148** generates the PFM_BOOST-d signal from its Q output. The PFM_BOOST-d signal is provided to one input of an OR gate **146** to generate a PFM_BOOST signal. The PFM_BOOST-d signal is provided to the gate of transistor **112** while the gate of transistor **110** is connected to the PFM_BOOST signal and the BUCK_HS and BUCK_LS signals are provided to the gates of transistors **106** and **108**, respectively.

To implement the STATE [3] wherein the inductor **114** is connected between node **103** and node **128** with switch **108** turned on and switch **106** turned off and switch **110** turned on with switch **112** turned off, a comparator **820** is provided having the inverted input connected to a reference voltage indicating the level at which the current through the inductor **114** has been discharged to a zero value, as indicated by the current sensor **119**. This is labeled $V_{ZEROLIMIT}$. The non-inverting input of comparator **820** is connected to the output of the current sensor **119**. The output provides a logic “high” signal when the current is indicated as being above zero value and a logic “low” when the current falls to a value at or below the zero value. The output of comparator **820** is labeled V_Z and is connected to the other input of the AND gate **822** which has the one input thereof connected to the output of the buffer **150**, the output of the AND gate **822** providing BUCK_LS output. When the current is determined to be below zero value, the output of the AND gate **822** is low and turns off transistor **108**. Similarly, the output of comparator **820** is connected to one input of the input OR gate **146**, which input is an inverted input, the other input of the OR gate **146** connected to the output of the SR latch **148** and receiving the PFM_BOOST-d signal, the output of the OR gate **146** driving the gate of transistor **110**. Thus, when the output V_Z of comparator **820** goes low, the V_Z signal input to the inverted input of OR gate **146** will cause the output PFM BOOST of the OR gate **146** to go high, thus turning off transistor **110**. Since the

output of OR gate **142** is high due to the voltage limit condition, this will result in a tri-state condition for the inductor **114**.

Referring now to FIG. 9, there is illustrated the operation of the buck-boost converter and associated control circuitry of FIG. 8 in buck-boost PFM operation of boost mode. For simplicity purposes, the node **122** will either be pulled to the voltage on node **118** or to the reference voltage on node **103** and will be referred to as being at a “high” level when at the voltage level of node **108** and at a “low” level when at the voltage level of node **103**. The signal at node **122** will be labeled SW1. Similarly, the signal at node **126** will be pulled up to the voltage level of the output node **128** or down to the voltage level of node **103**. The label for node **126** will be SW2 and, when the level is at the level of node **128**, it will be referred to as being disposed at a “high” level and, when disposed at the voltage level of node **103**, it will be referred to as being disposed at a “low” level. Both of the levels for nodes **122** and **126** will be represented as being at one of those two states or levels, it being understood that the state is in actuality a varying voltage level of either the reference voltage of node **103**, the input voltage level or the output voltage level for the respective node. Also, when all switches are off, the voltage on the nodes **122** and **126** will “float” at a three-state level, sometimes referred to as a tri-state condition.

At time T_1 , responsive to the clock signal going to a logical “high” level at the input of SR latch **148**, the PFM_BOOST-d signal at the output of the SR latch **148** goes from a logical “low” level to a logical “high” level. Switches **108** and **110** are turned off and switches **106** and **112** are turned on. This causes switching node (SW1) **122** to go to a “high” level and switching node (SW2) **126** to go to a “low” level. This will cause the inductor current I_L to begin increasing from time T_1 to time T_2 . At time T_2 , responsive to the current limit signal going to a “high” level, the PFM_BOOST-d signal will go from a logical “high” level to a logical “low” level. This causes the switching node SW2 (node **126**) to go to a “high” level while switching node SW1 (node **122**) remains at a “high” level when switch **110** turns on and switch **112** turns off. The inductor current I_L decreases from time T_2 to time T_3 . At time T_3 , responsive to a next clock signal, the PFM_BOOST-d signal goes from a logical “low” level to a logical “high” level turning off transistor **110** and turning on transistor **112** terminating the charge transfer operation before the inductor current has reached the zero crossing level and thus leaving the inductor current at a non-zero level. This causes switching node SW2 **126** to go to a “low” level while switching node SW1 **122** remains “high.” The inductor current then increases from the non-zero level from time T_3 to time T_4 in a subsequent inductor charge operation.

At time T_4 , a current limit signal causes the PFM_BOOST-d signal to go from a logical “high” level to a logical “low” level turning on transistor **110** and turning off transistor **112**, terminating the charge phase and initiating the next charge transfer phase. This causes switching node SW2 **126** to go to a “high” level while switching node SW1 **122** remains “high.” The inductor current I_L decreases from time T_4 to time T_5 during a charge transfer operation. At time T_5 , responsive to another rising clock edge, the PFM_BOOST-d signal goes from a logical “low” to a logical “high” level driving switching node **126** SW2 to a low level (close to GND) by turning off transistor **110** and turning on transistor **112** while switching node **122** SW1 remains at a high level (close to V_{IN}) at a non-zero inductor current level. The inductor current increases from the non-zero level from time T_5 to time T_6 . Responsive to another current limit signal at time T_6 , the PFM_BOOST-d signal will go from a logical “high” level to

9

a logical “low” level terminating the charge storage operation of the inductor. This again drives switching node **126** SW2 high (close to V_{OUT}) by turning on transistor **110** and turning off transistor **112**. The inductor current then decreases from time T_6 to time T_7 , T_7 occurring prior to the next clock edge.

At time T_7 , the voltage limit signal goes from a logical “low” to a logical “high” level driving BUCK_HS to a logic “high” level. This drives switching node SW1 **122** low when the voltage limit signal goes “high” while switching node SW2 **126** remains high (close to V_{OUT}) by turning off transistor **106** and turning on transistor **108**. The inductor current then decreases from time T_7 to time T_8 . Thus, the buck-boost PFM mode of operation within the circuit of FIG. 1 includes charge phases **202** in a first mode of operation and discharge phases **204** in a third mode of operation. However, these charge phases **202** and discharge phases **204** are separated by pass through phases **206** in a second mode of operation which eliminate a four switch switching condition. As can be seen with respect to switch node SW1 **122** and switch node SW2 **126** switching signals during the entire PFM period, there occurs no four switch switching conditions.

The implementation of FIG. 8 enables the pass through phase until a next clock signal is received at the input of SR latch **148** and the inductor current I_L is less than the PFM peak current limit or the voltage limit reaches a predetermined level for example 1.5% higher than a target value. If the clock edge occurs and the inductor current is less than the PFM peak current limit, the pass through will be followed by a charge phase as illustrated at time T_3 and time T_5 . If the voltage limit is reached during a pass through phase, a discharge phase is enabled to discharge the inductor current to zero and complete the PFM operation as illustrated at time T_7 .

Referring now to FIG. 10, there is illustrated a state diagram for the operation of the disclosed embodiment of FIGS. 8 and 9. In this embodiment, as described hereinabove, the charge operation sequences through STATE [1] and STATE [2] until the voltage limit is reached representing the target voltage, at which time the energy of the inductor **114** is fully transferred in a discharge operation in STATE [3]. Thus, the boost operation is initiated in a STATE [1] block **1001** and the proceeds along a path **1003** to STATE [2] at block **1005**. Until the voltage limit is reached, STATE [2] returns to STATE [1] at block **1001** through a path **1007**. This will continue until the target voltage has been reached at a V_{LIMIT} for the output voltage V_{OUT} . This state diagram will then go from STATE [2] at a block **1005** to STATE [3] at a block **1011**. Once I_L has been determined to equal zero, at a zero crossing, the state diagram will flow along path **1013** to a fourth state at block **1015** for STATE [4]. This state is the sleep state in which all switches are opened and the system will be maintained in this state until the voltage V_{OUT} falls below the target or desired voltage, at which time the state diagram will pass along a path **1017** back to STATE [1] at block **1001**.

The state diagram of FIG. 10 is illustrated in a timing diagram of FIG. 11. In this diagram, it can be seen that the states sequence through STATE [1] and STATE [2] until the voltage limit V_{LIMIT} has occurred at a point **1101**. At this point, the state diagram changes from STATE [2] to STATE [3] at a point **1103**. This will increase the discharge rate to a point **1105** at which time the zero crossing of the inductor current has been detected and STATE [4] will be entered thereafter. This will occur before the next clock edge. However, it should be understood that, if the voltage limit occurs close enough to the clock edge, it may be that the zero crossing does not occur before the next clock edge, but, since V_{LIMIT} has been reached, this will be overwritten and switch S1 will be maintained open and switch S2 will remain closed

10

until the zero crossing has occurred, at which time the system will pass to STATE [4] until the next clock edge.

Referring now to FIG. 12, there is illustrated an alternative embodiment of a buck-boost converter and control circuitry having improved PFM operation in the boost mode. The buck-boost converter **302** includes four switching transistors **306**, **308**, **310** and **312** and an inductor **314**. The input voltage V_{IN} is applied at an input voltage node **316**. A current sensor **318** monitors the input current applied through the input voltage node **316** and generates a signal I_{SNS} comprising a voltage associated with the input current and a current sensor **319** monitors the output current through transistor **310** to voltage node **328** and generates a signal I_{SNS} comprising a voltage associated with the output current. Transistor **306** has its source/drain path connected between node **320** and node **322**. A transistor **308** has its drain/source path connected between node **322** and a reference node **317** connected to a reference voltage such as ground. Inductor **314** is connected between node **322** and node **326**. Transistor **310** has its source/drain path connected between the output voltage node V_{OUT} **328** and node **326**. Transistor **312** has its drain/source path connected between node **326** and node **317**. A capacitor **330** is connected between node **328** and node **317**, and a resistor **332** is in parallel with the capacitor **330** between node **328** and node **317**. The gates of transistors **310** and **312** are connected to receive the PFM_BOOST and signals PFM-BOOST-d, respectively, from the control circuitry **304**.

The control circuitry **304** monitors the output voltage at node **328** using a resistor divider consisting of a resistor **334** connected between node **328** and node **336** and a resistor **338** connected between node **336** and ground. Node **336** provides the feedback voltage V_{FB} to a non-inverting input of a voltage comparator **340**. The inverting input of the voltage comparator **340** receives a reference voltage V_{REF} . The output of the voltage comparator **340** generates a voltage limit signal that is provided to a first input of an OR gate **342**.

The other input of OR gate **342** is connected to receive a current limit signal V_{LIMIT} from the output of a voltage comparator **344**. The voltage comparator **344** receives the I_{SNS} voltage signal from the current sensor **318** at its non-inverting input and the VILIM voltage limit signal at its inverting input. The output of the OR gate **342** is connected to the R input of SR latch **348**. The SR latch **348** is reset dominant to prevent the clock signal CLK from setting the latch if its reset R input is logic “high”, implementing pulse skipping, a form of PFM control. The output of OR gate **342** will generate a logical “high” value responsive to either the voltage limit signal or the current limit signal from the output of comparators **340** and **344**, respectively, going to a logical “high” level. The voltage limit signal goes to a logical “high” level when the feedback voltage V_{FB} exceeds the reference voltage V_{REF} . The current limit signal goes to a logical “high” level when the I_{SNS} signal from the current sensor **318** exceeds the VILIM voltage.

The SR latch **348**, in addition to receiving the output of the OR gate **342** at its R input receives a clock signal (CLK) at its S input. Responsive to the CLK signal and the output of the OR gate **342**, the Q output of the SR latch **348** is connected to one input of an OR gate **1226**, the output thereof generating the PFM_BOOST signal. The Q output of the latch **348** is also connected to the input of a buffer **346** to generate a PFM-BOOST-d signal. The Q output of the SR latch **348** is input to the input of a fixed rising edge delay timer **350**. The fixed rising edge delay timer **350** adds a delay to the PFM_BOOST-d signal and is input to one input of an AND gate **1224** to provide at its output the BUCK_LS signal, which is provided to the gate of transistor **308**. The output of the delay

11

timer 350 is also provided as an input to a buffer 352. The output of the buffer 352 provides the BUCK_HS signal. The PFM_BOOST-d and PFM-BOOST signals are provided to the gates of transistors 312 and 310, respectively, while the BUCK_HS signal is provided to the gate of transistor 306.

The control circuit 304 inserts a pass through phase after the charge phase that will last for a “fixed” period of time that is followed by the discharge phase. This method, while not eliminating the four switch switching conditions as occurs with respect to the implementation of FIG. 9, greatly reduces the number of four switch switching conditions which improves the overall efficiency of the buck-boost converter.

Referring further to FIG. 12, when the current through the inductor 314 is at a zero value in STATE [3], it is necessary to turn off transistor 308 and transistor 310. A comparator 1220 has the inverting input connected to a limit voltage $V_{ZEROLIMIT}$ and the non-inverting input connected to the output of the current sensor 319. When the inductor current is determined to have gone below the zero limit value, the output of the comparator 1220 will go low. The output of comparator 1220 is labeled V_Z , which is connected to the other input of the AND gate 1224. When V_Z goes low, the output of AND gate 1224 will go low, turning off transistor 308. Similarly, the OR gate 1226 has an inverted input connected to the output of the comparator 1220, V_Z . Thus, when V_Z falls low, the output of OR gate 1226 will be high which will turn off transistor 310, the P channel transistor. Thus, when zero current limit is exceeded and the voltage limit has been exceeded, the output of comparator 1220 being low and the output of comparator 340 being high will result in a tri-state condition for all of the switches. Further, the voltage limit being exceeded will also keep the SR latch 348 in a low output condition such that a rising clock edge will not perform a reset thereon.

Referring now to FIG. 13, there is illustrated the operation of the buck-boost converter and control circuitry of FIG. 12 that includes a fixed pass through phase of operation after each charge phase. Responsive to a clock edge at time T_1 , the PFM_BOOST and PFM-BOOST-d signals go from a logical “low” level to a logical “high” level causing switch 310 to turn off and transistor switch 312 turned on. This causes the voltage at switching node SW1 (node 322) to go to high level as switch 306 is turned on and switch 308 is turned off, and the voltage at switching node SW2 (node 326) to go to low level responsive to transistor 310 turning off and transistor 312 turning on. The inductor current I_L begins increasing from time T_1 to time T_2 . At time T_2 , responsive to a logical “high” level of the current limit signal from the output of voltage comparator 344, the voltage at switching node SW2 (node 326) goes from a low level to a high level as switch 310 turns on and switch 312 turns off. This initiates a pass through period from time T_2 to time T_3 when the inductor current I_L is decreasing and energy is transferred to the load. The period from time T_2 to time T_3 is a fixed on time established by the fixed rising edge delay timer 350. After expiration of the fixed on time at time T_3 , the output signal of the delay timer 350 goes from a logical “low” to a logical “high” level causing the voltage at node SW1 (node 322), as transistor 306 turns off and transistor 308 turns on, to go from high to low level. The inductor current I_L goes through a discharge phase from time T_3 to time T_4 or until a zero crossing occurs.

At time T_4 , responsive to a rising clock edge, the PFM_BOOST signal goes from a logical “low” level to a logical “high” level causing switches 308 and 310 to turn off and switches 306 and 312 to turn on. This causes the voltage at switching node SW1 (node 322) to go from low level to high level and the voltage at switching node SW2 (node 326) to go

12

from high to low level. This causes a four switch switching condition. The inductor current goes through another charge phase from time T_4 to time T_5 . At time T_5 the PFM_BOOST signal goes from a logical “high” to a logical “low” level causing the voltage at switching node SW2 (node 326) to go from low to high level when switch 310 turns on and switch 312 is turned off. This initiates the pass through phase from time T_5 to time T_6 when the inductor current I_L will decrease.

The pass through phase is for a fixed on time from time T_5 to time T_6 based upon the output of the fixed rising edge delay timer 350. After the fixed on time from time T_5 to time T_6 , the voltage at node SW1 will go from high to low level responsive to switch 306 turning off and switch 308 turning on beginning initiation of the discharge phase at time T_6 to time T_7 . At time T_7 , another rising clock edge causes the PFM_BOOST signal to go from a logical “low” to a logical “high” level causing transistors 310 and 308 to turn off, transistors 306 and 312 to turn on, and the voltage at switching node SW1 (node 322) to go from low to high level while the voltage at switching node SW2 (node 326) goes from high to low level. This initiates the next charge period and a four switch switching condition occurs at time T_7 .

The circuit of FIG. 12 includes a number of charge phases 402 in a first mode of operation and discharge phases 404 in a third mode of operation that are each separated by a fixed length pass through phase 408 in a second mode of operation. As can be seen with respect to the switching signals, a reduced number of four switch switching conditions occur at points 410 within the switching cycle of the switching transistors. This improves the efficiency of the operation of the circuit of the buck-boost converter, though not as much as that described with respect to FIG. 8.

Referring now to FIG. 14, there is illustrated a state diagram depicting the operation of FIGS. 12 and 13 and the disclosed embodiment therein. The state diagram in FIG. 14, is initiated at a state block 1401 for STATE [1] and then flows to a block 1403 for STATE [2] along a path 1405. However, as noted hereinabove, after a predetermined time delay, the state will change from STATE [2] to STATE [3] at a block 1406 along a path 1407. At the next clock cycle, the state will change from STATE [3] to STATE [1] at the block 1401 along a path 1409. The state will continue to flow on paths 1405, 1407 and 1409 until a voltage limit is achieved. At this time, the state will be maintained within STATE [3] at block 1406 until the current to the inductor is equal to a zero value, i.e., it crosses zero. At this point, the state will change from STATE [3] at 1406, wherein switch S2 is closed and S1 is opened and S3 is closed and S4 is opened until such occurs. At this time, the state diagram will change to STATE [4] at a block 1411 along a path 1413. The system will remain in this state until the voltage falls below the V_{LIMIT} target value, at which time the state will change to STATE [1] at block 1401 along a path 1415.

The timing flow of the state diagram of FIG. 14 is illustrated in FIG. 15. In this operation, it can be seen that STATE [2] is maintained for a predetermined amount of time, T_D . Thus, the clock edge initiates STATE [1], and the current of the inductor current I_L equaling the current limit value, I_{LIMIT} results in the change from STATE [1] to STATE [2]. At the end of the fixed delay, the system changes to STATE [3]. During the operation wherein the voltage has not reached the voltage limit, V_{LIMIT} , the next charging cycle will occur at the next clock cycle, i.e., STATE [1] will again be entered. This is a flow along paths 1405, 1407, and 1409. However, once V_{LIMIT} is reached, then STATE [3] is forced to remain the existing state until the current charging the inductor has

13

decreased to a zero value, even if the next clock edge occurs during that time. The system mode then goes to STATE [4] at a point 1501.

Referring now to FIG. 16, there is illustrated an upper level block diagram of the buck operation. The buck-boost controller 105 is comprised of two operations, as described hereinabove, the boost operation and the buck operation. Thus, there will be a control section associated with the boost operation, that being the boost controller 104 described hereinabove with respect to control of the boost operation. There will also be provided a buck controller 1602, which is operable to control the buck operation. In the buck operation, the H-Bridge 101 is controlled such that the buck side of the H-Bridge 101 is controlled to alternately switch S1 and S2 to a closed or open position in accordance with a buck operation and switch S4 will be maintained open and switch S3 maintained closed on the boost side of the H-Bridge 101. For a standard buck operation, inductor 114 is charged by connecting the buck side of the inductor 114 to V_{IN} through switch S1. Once charged, the charge is transferred by opening switch S1 and closing switch S2 and connecting the buck side of the inductor 114 to the reference voltage or ground. The charging operation increases the inductor current to the predetermined current limit and then switches to a discharge or charge transfer operation to reduce the inductor current to a zero value. This operates in accordance with a PFM operation.

With further reference to FIG. 16A, there is illustrated a timing diagram for the operation of the buck controller 1602. A fixed frequency is provided by the clock circuit 107 wherein a clock edge will initiate a PFM charging operation to close switch S1 and open switch S2, switch S4 remaining open and switch S3 remaining closed. This charging operation will continue until a point 1610 at which time a maximum current limit has been reached. This will switch the operation over to a discharge or transfer mode in which energy is transferred to the load from the inductor 114. This transfer will continue until the current through the inductor is zero, as determined by the buck controller 1602 by sensing the current through transistor 310 with the current sensor 119. At this point, point 1612, the switches S1-S4 will be placed in a tri-state mode and all of the switches will be opened. At the next clock edge, 1614, the next charge operation will occur. This will continue until a voltage limit is determined as having been reached, as indicated by a voltage limit signal 1616. At this time, what will occur is that the switches will be maintained in the tri-state mode and the next clock edge will not initiate another charge operation. If the voltage limit signal 1616 occurs before the current through inductor 114 has decreased to a zero value, the tri-state mode will be delayed until such occurrence, after which all switches will be placed in tri-state mode.

With further reference to FIG. 16, it is noted that a comparator 1618 with hysteresis is provided to compare the input and output voltages. This determines whether the boost mode has moved into the transition buck or boost area as described hereinabove with respect to FIG. 2A. The hysteresis will allow the determination to be made as to whether the input voltage is less than the output voltage by dV_1 or is greater than V_{OUT} by a value of dV_2 . If so, then the boost mode will switch to the buck mode or the buck mode will switch to the boost mode. The boost mode will be maintained until the input voltage is greater than the output voltage by dV_2 and the buck mode will remain in the buck mode until dV_1 decreases below the output voltage.

Voltage regulators and associated circuitry according to the embodiments of the present disclosure can be embodied as a variety of different types of electronic devices and systems,

14

such as computers, cellular telephone, personal digital assistants, and industrial systems and devices. More specifically, some applications include, but are not limited to, CPU power regulators, chip regulators, point of load power regulators and memory regulators. FIG. 17 is a block diagram of an electronic/electric system or functional device 1702. The functional device 1702 is a device that requires a regulated voltage at a particular and set voltage, this being defined by the operating parameters of the device 1702. For illustrative purposes, the device 1702 includes certain operating blocks such as a CPU 1712, a memory 1716, a clock or timing circuit 1714 that operate together to provide an integrated application specific device. This can be entirely realized in silicon on an integrated circuit or it can be formed of discrete devices. A data bus 1722 is provided to allow communication between components within the device 1702.

To provide power to the device, an external voltage V_{IN} is input to a buck-boost regulator 1701 operating in either a buck mode or a low ripple PFM boost mode. The input voltage can operate over a much larger range than the device operating voltage, such that the regulator 1701 must accommodate voltages that range from voltages below the operating voltage to voltages above the operating voltage. The operating voltage is labeled V_{OUT} and is illustrated as powering the CPU 1712 and the clock 1714. It is also illustrated as powering a USB driver 1718 that interfaces with an external USB device 1704. For this operation, power from the regulator 1701 is used to power the external USB device 1704. Additionally, there are other external devices that can be interfaced to the device 1702, such as input devices 1706, such as a keyboard and scanner, etc., and output devices 1708 such as an LCD display. Further, external storage 1710 can be accommodated in the form of Flash drives, hard drives, DVDs, etc. These are interfaced with the data bus 1722. There is provided an I/O 1720 to interface between the components on the device 1702 and the input and output devices to provide the various drivers and the such. All of the external devices could be interfaced with the USB driver 1718, providing they are USB interfaceable devices. The regulator 1701 utilizes the PFM boost circuitry described hereinabove to achieve an improved efficiency and lower ripple.

It will be appreciated by those skilled in the art having the benefit of this disclosure that this system and method for high efficiency PWM control of buck-boost converter provides a more efficiently operating buck-boost converter. It should be understood that the drawings and detailed description herein are to be regarded in an illustrative rather than a restrictive manner, and are not intended to be limiting to the particular forms and examples disclosed. On the contrary, included are any further modifications, changes, rearrangements, substitutions, alternatives, design choices, and embodiments apparent to those of ordinary skill in the art, without departing from the spirit and scope hereof, as defined by the following claims. Thus, it is intended that the following claims be interpreted to embrace all such further modifications, changes, rearrangements, substitutions, alternatives, design choices, and embodiments.

What is claimed is:

1. A DC-DC converter, comprising:

an input terminal for receiving an input voltage from an input voltage source disposed at an input voltage level;
an output terminal for providing an output voltage at an output voltage level different than the input voltage level to a load connected to the output terminal;
an energy storage element for receiving and storing energy from the input voltage source on an input side thereof via

15

the input terminal and transferring at least a portion of the stored energy to the load from an output side thereof; and

a control system for controlling the storage of energy to and transfer of energy from the energy storage element in at least three recurring phases to attain a desired level for the output voltage level, the three phases comprising an energy storage phase for storing energy from the input terminal in the energy storage element, a first energy transfer phase for transferring only a portion of the stored energy from the energy storage element to the load, and a second energy transfer phase to transfer substantially all of the energy to the load, the control system for initiating the second energy transfer phase in response to a magnitude of the output voltage equaling or exceeding a magnitude of the desired level for the output voltage.

2. The converter of claim 1, wherein the energy storage element comprises an inductor.

3. The converter of claim 1, and further comprising a clock circuit having a fixed frequency and wherein the energy storage phase and the first energy transfer phase are controlled by the control system to occur in a single period of the clock, with the end of the first energy transfer phase occurring at the end of the clock period.

4. The converter of claim 3, wherein the control system is for initiating the second energy transfer phase in response to a condition of the output voltage independent of the clock.

5. The converter of claim 4, further comprising a comparator for determining that the condition exists in response to the magnitude of the output voltage equaling or exceeding the magnitude of the desired level for the output voltage.

6. The converter of claim 3, wherein the energy storage phase stores energy in the energy storage element until a predetermined amount of energy is stored therein, such that the length of time for reaching the predetermined amount of energy varies as a function of the initial amount of energy stored therein at the beginning of the energy transfer phase and the length of time for the first energy transfer phase will change accordingly.

7. The converter of claim 6, wherein the energy storage element comprises an inductor and the predetermined amount of energy is defined by a current limit of the current through the inductor during charging thereof in the energy storage phase.

8. The converter of claim 1, wherein the desired level of the output voltage is higher than the input voltage to provide a boost DC-DC conversion operation.

9. The converter of claim 1, wherein the energy storage element comprises an inductor and the control system comprises:

a switching bridge having first and second switching nodes, each connected to opposite sides of the inductor with a set of first and second input switches for connecting the first switching node to the input terminal with the first input switch and to a reference voltage with the second input switch and a set of first and second output switches for connecting the second switching node to the output terminal with the first output switch and to a reference voltage with the second output switch; and
a switch controller controlling the first and second input switches and first and second output switches to connect the inductor between the input terminal and the reference voltage and, in the first energy transfer phase, to connect the inductor between the input and output ter-

16

minals and, in the second energy transfer phase, to connect the inductor between the reference voltage and the output terminal.

10. A DC-DC converter, comprising:

an input terminal for receiving an input voltage from an input voltage source disposed at an input voltage level; an output terminal for providing an output voltage at an output voltage level different than the input voltage level to a load connected to the output terminal;

an energy storage element for receiving and storing energy from the input voltage source on an input side thereof via the input terminal and transferring at least a portion of the stored energy to the load from an output side thereof;

a control system for controlling the storage of energy to and transfer of energy from the energy storage element in at least three recurring phases to attain a desired level for the output voltage level, the three phases comprising an energy storage phase for storing energy from the input terminal in the energy storage element, a first energy transfer phase for transferring only a portion of the stored energy from the energy storage element to the load and a second energy transfer phase to transfer substantially all of the energy to the load;

a clock circuit having a fixed frequency and wherein the energy storage phase and the first energy transfer phase are controlled by the control system to occur in a single period of the clock, with the end of the first energy transfer phase occurring at the end of the clock period; and

wherein the control system sequences the operation of the energy storage phase followed by the first energy transfer phase during sequential periods of the clock until the external condition occurs, such that at the end of a preceding period of the clock, there will be a non zero energy level in the energy storage element and the energy storage phase of a current period will charge the energy storage element from the non zero energy level until the occurrence of the external condition.

11. A buck-boost DC-DC converter, comprising:

an input terminal connected to an input voltage source operating at an input voltage level;

an output terminal connected to a load;

a reference node disposed at a reference voltage level;

a buck-boost conversion circuit, including:

an inductor,

a buck switching section for transferring energy to the inductor and subsequently transferring energy to the load on the output terminal in a voltage buck conversion operation, and

a boost switching section for transferring energy to the inductor and subsequently transferring energy to the load on the output terminal in a voltage boost conversion operation; and

a buck-boost controller for controlling at least the boost switching section to operate in a Pulse Frequency Modulation (PFM) boost mode of operation, the controller including:

a clock operating at a fixed frequency, and

a phase controller to control first and second output switches to operate in a charging phase initiated at an edge of the clock to connect the inductor between the input terminal and the reference voltage node to charge the inductor to a predetermined energy level and then operate in a first energy transfer phase to connect the inductor between the input terminal and the output terminal to transfer energy from the inductor and the input terminal to the output terminal until

17

the occurrence of the next clock edge, wherein the inductor will be at a non zero stored energy level.

12. The converter of claim 11, wherein the buck-boost controller includes a comparator for comparing the voltage level on the output terminal to a desired reference voltage and, when the voltage level on the output terminal equals or exceeds the reference voltage, the phase controller operates the boost switching section and the buck switching section in a second energy transfer phase to connect the inductor between the reference node and the output terminal to transfer substantially all of the energy stored in the inductor to the output terminal to reduce the energy therein to a substantially zero value.

13. The converter of claim 12, wherein the buck-boost controller controls the boost switching section and the buck switching section to disconnect the inductor from the input and output terminals and the reference node at the end of the second energy transfer phase.

14. The converter of claim 11, wherein the buck-boost controller controls the buck switching section to operate in a PFM buck mode of operation.

15. The converter of claim 14, and further comprising a mode comparator to compare the voltage levels on the input and output terminals and switching between buck and boost modes of operation when the two voltages are within a predetermined voltage.

16. The converter of claim 11, wherein the buck-boost controller further includes a current limit detector to detect the flow of current into the inductor and change phase from the charge phase to the first energy transfer phase when a predetermined inductor current is detected in the charge phase.

17. A method for controlling operation of a buck/boost regulator, the method comprising:

generating a regulated output voltage on an output node responsive to an input voltage received on an input node and a plurality of control signals;

monitoring the regulated output voltage; and

generating a plurality of control signals responsive to the output voltage, wherein the plurality of control signals include a first mode of operation controlling a charge phase of the buck/boost regulator to charge an energy storage element from the input voltage on the input node, a second mode of operation controlling a pass through phase of the buck/boost regulator to both transfer stored energy from the energy storage element to the output node and transfer energy from the input node to the output node, and a third mode of operation controlling a discharge phase of the buck/boost regulator to fully transfer the stored energy in the energy storage element to the output node via a conduction path of at least one closed switch, a conductance of the conduction path responsive to one of the control signals;

wherein the plurality of control signals control the buck/boost regulator to eliminate occurrence of a four switch switching condition.

18. The method of claim 17 further including:

generating the regulated output voltage responsive to an input voltage and the plurality of control signals at the buck/boost regulator; and

operating the buck/boost regulator according the plurality of control signals in one of the first, second or third modes of operation.

19. The method of claim 18, wherein the operating further comprises:

controlling a plurality of switching transistors in the buck/boost regulator to enable a charging phase in the first

18

mode of operation responsive to a clock signal and a current limit signal to charge an inductor to the current responding to the current limit signal; and

controlling the plurality of switching transistors in the buck/boost regulator to enable a pass through phase in the second mode of operation responsive to the clock signal and the current limit signal to both transfer energy stored in the inductor to the output node and transfer current from the input node to the output node such that only a portion of the stored energy in the inductor is transferred to the output node.

20. The method of claim 19, wherein the operating further comprises controlling the plurality of switching transistors to enable a discharge phase in the third mode of operation responsive to a voltage limit signal to fully transfer the energy stored in the inductor to the output node with no energy transferred to the output node from the input node.

21. A method for controlling operation of a buck/boost regulator, comprising:

generating a regulated output voltage on an output node responsive to an input voltage received on an input node and a plurality of control signals;

monitoring the regulated output voltage;

generating a plurality of control signals responsive to the output voltage, wherein the plurality of control signals include a first mode of operation controlling a charge phase of the buck/boost regulator to charge an energy storage element from the input voltage on the input node, a second mode of operation controlling a pass through phase of the buck/boost regulator to both transfer stored energy from the energy storage element to the output node and transfer energy from the input node to the output node, and a third mode of operation controlling a discharge phase of the buck/boost regulator to fully transfer the stored energy in the energy storage element to the output node via at least one closed switch; wherein the plurality of control signals control the buck/boost regulator to eliminate occurrence of a four switch switching condition;

generating a voltage limit signal indicating when the regulated output voltage exceeds a reference voltage;

generating a current limit signal indicating when an input current to the energy storage element during the charge phase of the buck/boost voltage regulator exceeds a predetermined current limit reference signal;

generating a first portion of a plurality of control signals to control a pair of boost switching transistors of a plurality of switching transistors that switch one side of the energy storage element to a reference voltage during the charge phase and to the output node during the pass-through phase and discharge phase associated with the buck/boost regulator responsive to the voltage limit reference signal, the current limit signal and a clock signal; and

generating a second portion of the plurality of control signals to control a pair of buck switching transistors of the plurality of switching transistors associated with the buck/boost regulator that connect another side of the energy storage element to either the reference voltage during the discharge phase or the input node during the pass-through phase responsive to the voltage limit signal.

22. A system, comprising:

a buck/boost voltage regulator for generating a regulated output voltage on an output node responsive to an input voltage received on an input node and drive control

signals, the buck/boost voltage regulator including a plurality of switching transistors;
control circuitry for monitoring the regulated output voltage and generating the plurality of drive control signals responsive thereto, wherein the control circuitry controls the operation of the plurality of switching transistors to enable a charging phase in a first mode of operation to store energy in an inductor from the input node, a pass through phase in a second mode of operation to transfer only a portion of the energy stored in the inductor to the output node and transfer energy from the input node to the output node, and a discharge phase in a third mode of operation where the energy in the inductor is fully transferred to the output node via at least an on one of the switching transistors to eliminate occurrence of a four switch switching condition; and
a load coupled to the output of the buck/boost voltage regulator.

23. The system of claim **22**, wherein the load is selected from a group consisting of a processor, a memory, an input device, an output device and a storage device.

* * * * *