Title: WASTE ENERGY CONTROL MANAGEMENT FOR POWER AMPLIFIER

An amplifying apparatus for linearly amplifying a desired signal using a pair of coupled non-linear amplifiers (57) is disclosed. The amplifying apparatus comprises a limiter (21) for separating amplitude variations from the desired signal and producing a constant amplitude signal bearing the phase of the desired signal and an amplitude related signal. In addition, a drive signal generator (62) produces two drive signals each dependent on the constant amplitude signal and the amplitude related signal such that each drive signal depends on the phase of the desired signal and such that the sum of the squares of the amplitudes of the drive signals is constant. Finally, a coupler (56) couples the two drive signals to produce two constant amplitude signals for driving the pair of non-linear power amplifiers (57) and for coupling the outputs of the power amplifiers (57) to produce two amplified output signals, one of which is the linearly amplified desired signal and the other of which is a waste energy signal.
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WASTE ENERGY CONTROL MANAGEMENT FOR POWER AMPLIFIER

Field of the Disclosure
The present invention relates to class C matrix power amplifiers for use in cellular radio communication systems, and particularly to a satellite cellular radio communication. In addition, the present invention relates to methods for recovering energy that would otherwise be wasted energy in certain power amplifier/antenna combinations.

Background of the Disclosure
In conventional satellite communications systems, transponders formerly consisted of a number of separate power amplifiers each carrying multiple signals. The operating point of each amplifier was normally set to produce an average output level substantially below the saturated output level of the amplifier in order to maintain linear operation.

However, U.S. Patent No. 3,917,998 to Welti entitled "Butler Matrix Transponder" describes an arrangement of N coupled power amplifiers for amplifying N signal paths. The N signal paths envisaged comprise the relaying of signals from at least one ground station to N locations on the earth using an orbiting satellite. The benefit of using coupled amplifiers over using a set of N non-coupled amplifiers is that the set of non-coupled amplifiers is limited to generating a power which does not exceed the peak power capability of a single amplifier in any signal path, whereas the technique which uses coupled amplifiers allows the generation of a power equal to the sum of the powers of all the amplifiers in any signal path.

provided that all signal paths do not require higher than the mean power at the same time. As a result, signals that vary both above and below a mean power level are accommodated more efficiently due to a better statistical averaging of the power demanded by the N signal paths. The matrix power
amplifier of the Welti patent is for use in frequency division multiple access (FDMA) applications, and provides the facility to vary the number of FDMA carrier frequencies used in each signal path and thus correspondingly the power needed in each signal path over a wide range.

A matrix power amplifier according to the Welti patent contains a butler matrix for combining a number N of input signals to be amplified to produce N different combinations of the input signals. In addition, a set of N power amplifiers are provided so that each amplifier amplifies one of the combinations to produce N amplified signals. The matrix power amplifiers also contain a butler matrix for combining the amplified signals to produce N outputs that are amplified versions of the original N input signals. The benefit as compared with simply amplifying the original N inputs in independent amplifiers is the ability, if instantaneously needed, to devote more than the power of a single amplifier to one of the N signal paths. In principle, the matrix power amplifier can deliver the sum of the power output of all amplifiers to a single output.

The characteristics of intermodulation generated by non-linearities in a matrix power amplifier are different than in a single amplifier. It can be shown that third order intermodulation between signals input respectively to inputs I and J of the input butler matrix appears on the output numbers (2i - j)_n and (2j - i)_n of the output butler matrix. As a first step to reducing intermodulation in a matrix power amplifier, one embodiment of the present invention provides an excess number of amplifying paths so that outputs (2i - j) or (2j - i) or their corresponding inputs are not used for desired signal outputs, but are terminated in dummy loads. Thus, third order modulation between signals i and j will not be transmitted. This requires that the number of butler matrix input and output ports M be greater than the number of signals to be amplified N, wherein the remaining M - N signals are terminated in dummy loads.
It is easy to see that if only two signals are to be amplified, then using ports 1 and 2 as inputs and outputs will result in third order intermodulation appearing on ports 0 and 3, which are terminated. It is not so obvious how to achieve this when many signals are present. This problem is however solved by Babcock in another context. Babcock wanted to find a method of allocating frequency channels on an equally spaced grid to signals amplified by the same non-linear amplifiers such that third order intermodulation between any two or three signals would not fall in a channel used by a signal. The mathematical formulation of the problem is the same as for the inventive matrix power amplifier, wherein a set of integers is found $I_1, I_2, I_3\ldots$ such that $I_i + I_k - I_j$ is not in the set. The solution is called "Babcock spacing". Babcock applied these integers to choosing among $M$ frequency channels for the transmission of signals. However, the present invention applies Babcocks integer sets to choosing among $M$ physical output channels which are used for $N$ desired signals.

Consequently, the first improvement over the prior art matrix power amplifier according to the present invention is to employ a larger matrix than the number of signals to be amplified, and to allocate input and outputs to signals or not according to the Babcock spacing or other optimum allocation, thus insuring that intermodulation emerges principally from outputs that are not allocated to signals.

Furthermore, in the present cellular communications market, there is an emphasis on making mobile telephones small, handheld units which operate from attached, rechargeable batteries. A parameter of great interest to the user of such phones is the length of time that can be spent in conversation without needing to change or recharge the battery. This parameter is simply known as the "talk-time" offered by different types of mobile phones. Of course, it is possible to offer a longer talk-time by using bigger batteries, but the bigger batteries increase the size and weight of the mobile telephone. Therefore, designers and inventors strive to construct
devices which achieve longer talk-times for a given battery capacity. During a conversation, the radio transmitter power amplifier is the dominant power consumer. The efficiency of the amplifier's conversion of battery energy into radio energy thus has a direct bearing on the length of available talk-time for a cellular mobile telephone.

Cellular telephone systems were first introduced using analog frequency modulation to impress a voice on a radio signal. Analog frequency modulation has the advantage of producing a constant amplitude signal whose phase angle changes. The most efficient transmit power amplifiers can be constructed for constant amplitude signals which operate in a saturated output mode.

Original cellular systems using analog frequency modulation were also duplex, meaning that they received a signal in the reverse direction at the same time as transmitting a signal. A device known as a duplexer was therefore needed to couple both the transmitter and the receiver to the same antenna so as to avoid interference. As shown in Figure 1(a), the antenna 12 is connected to the duplexer 16, which is formed by the filters 11 and 13. The duplexer 16 then controls the signals to and from the power amplifier 10 and the receiver 14 so as to avoid interference. Figure 1(b) illustrates the addition of an isolator 15 in the transmit path which is used in some cases to protect the transmitter against antenna mismatches and/or to protect the transmitter from other signals picked up on the antenna and fed back to the transmitter causing an undesired phenomenon known as back-intermodulation. The isolator 15 diverts signals reflected from the antenna mismatches or received from other sources into a dummy load 18. The prior art does not disclose recycling of the energy diverted to the dummy load in order to increase the talk-time of handheld radios. A transmitter power amplifier illustrated in Figure 1(a) can be a single power amplifier.

A transmitter power amplifier can also be constructed by combining two similar, smaller sized amplifiers. If the amplifier devices are driven in
antiphase and their outputs are combined with a 180 degree relative phase so that their outputs add constructively, the amplifier is known as a push-pull amplifier. Sometimes, two similar amplifiers 20 and 21 can be driven 90 degrees out of phase and their outputs combined using a 90 degree or 
5 quadrature coupler as illustrated in Figure 2. The quadrature coupler 23 can 
be formed by running two strip transmission lines in parallel proximity to 
each other. The energy is transferred between the lines in such a manner that a signal flowing from left to right on one line induces a signal flowing from right to left on the other line but with a 90 degree phase shift. Thus, 
10 two amplifiers connected respectively to the left hand end of a first line and 
the right hand end of a second line will produce signals travelling from left 
to right on the first line and from right to left on the second line.

When the amplifiers are approximately driven 90 degrees out of 
phase, the net signal flowing on the first line becomes a sum signal and the 
15 net signal flowing on the second line is a difference signal, which can be 
arranged to be zero. The output of the difference line is usually terminated 
in a dummy load 24 which normally dissipates no power. Practical 
tolerances of the matching between the amplifiers, the accuracy of the phase 
shift, energy at harmonic frequencies or antenna mismatch at the sum line 
20 output can however result in significant energy dissipation in this dummy 
load. The prior art does not disclose recycling this otherwise wasted energy 
in order to increase the talk-time of a handheld radio.

Yet another configuration of a power amplifier, known as a 
feedforward amplifier, may be employed in some circumstances, in which 
25 linear power amplification rather than saturated power amplification of class 
C amplifiers is desired. In feedforward power amplifier configurations, a 
more or less non-linear amplifier 30 produces an output signal that is then 
corrected by adding an error signal, which is produced by an error amplifier 
31, to the output signal using a directional coupler 32 as described above and 
30 as is shown in Figure 3. A waste energy signal normally produced in
dummy load 33 corresponds to the unwanted difference signal. The unwanted difference signal is always produced when two dissimilar signals having overlapping spectra are added together. Again, the prior art does not disclose the recycling of the waste energy produced by the difference signal in order to increase talk-time.

**Summary of the Disclosure**

It is an objective of the present invention to overcome the deficiencies of the prior art and to provide an effective means to amplify multiple signals to a transmitted power level using power amplifiers adapted for efficiently amplifying signals of constant amplitude, such as Class C amplifiers, while avoiding high levels of intermodulation products.

One embodiment of the present invention discloses an amplifying apparatus for linearly amplifying a desired signal using a pair of coupled non-linear amplifiers. The amplifying apparatus comprises limiting means for separating amplitude variations from the desired signal and producing a constant amplitude signal bearing the phase of the desired signal and an amplitude related signal. In addition, a drive signal generation means produces two drive signals each dependent on the constant amplitude signal and the amplitude related signal such that each drive signal depends on the phase of the desired signal and such that the sum of the squares of the amplitudes of the drive signals is constant. Finally, a coupling means couples the two drive signals to produce two constant amplitude signals for driving the pair of non-linear power amplifiers and for coupling the outputs of the power amplifiers to produce two amplified output signals, one of which is the linearly amplified desired signal and the other of which is a waste energy signal.

Another embodiment of the present invention relates to a system for communicating using a first station with a first plurality of second stations using a phased array antenna. The system comprises signal generating
means for generating a first plurality of signals for transmission to respective second stations using radio wave modulation. Combining means then produce a second plurality of combined signals which are complex weighted sums of the first plurality of signals, wherein the second plurality corresponding to the number of antenna array elements disposed along a first dimension of the phased array. In addition, drive signal generation means produce from each of the second plurality of signals a third plurality of signals, the number of which corresponding to different groups of elements disposed along a second dimension of the phased array. Amplifying means are provided for amplifying the second plurality of signals with the third plurality of signals using respective transmit power amplifiers adapted to transmit constant amplitude signals. Finally, an antenna means is connected to the amplifying means such that wanted signals are radiated in desired directions and unwanted signals are dissipated in other directions.

In another embodiment of the present invention, the present invention relates to methods of transponding a multiplicity of TDMA signals from a satellite in a satellite communications system, and in particular to an arrangement of the satellite power amplifiers so as to provide some flexibility for raising the power level in certain TDMA time-slots.

It is another object of the present invention to overcome the problems cited above by recovering the waste energy produced by the power amplifier in order to increase the amount available talk time for a handheld mobile telephone. One embodiment of the present invention relates to a device for increasing the energy efficiency of an amplifier using feed forward linearization. The device comprises a direct current power source which provides power to the amplifier which produces a main output signal. A second amplifier amplifies an error signal. A combining network then combines the error signal with the main signal to produce a corrected sum signal and a wasted energy signal. Finally, a rectifier converts the wasted
energy signal into a direct current that is coupled back to the direct current power source in order to reduce the net power consumption.

**Detailed Description of the Drawings**

These and other features and advantages of the invention will be readily apparent to one of ordinary skill in the art from the following description, used in conjunction with the drawings, in which:

- Figures 1(a)-(b) illustrate a conventional power amplifier coupling to an antenna;
- Figure 2 illustrates a conventional quadrature coupled amplifier;
- Figure 3 illustrates a conventional feed forward linearization amplifier attached to an antenna;
- Figure 4 illustrates an over-dimensioned matrix power amplifier according to one embodiment of the present invention;
- Figure 5 illustrates a Class C linear power amplifier according to one embodiment of the present invention;
- Figure 6 illustrates an N channel matrix power amplifier using two N Class C amplifiers according to one embodiment of the present invention;
- Figure 7 illustrates a general Class C matrix power amplifier according to one embodiment of the present invention;
- Figure 8 illustrates a signal generator for producing phase modulated drive signals according to one embodiment of the present invention;
- Figure 9 illustrates a cylindrical array of slot antennas and a phase or a base station;
- Figure 10 illustrates a transmit array processor according to one embodiment of the present invention;
- Figure 11 illustrates a block diagram of a heat reduction method according to one embodiment of the present invention;
- Figure 12 illustrates a block diagram of the recovery of reflected power according to one embodiment of the present invention;
Figure 13 illustrates a graph showing the effective transmitter efficiency versus the antenna mismatch with and without one embodiment of the present invention;

Figure 14 illustrates in a graph the increase in talk time using one embodiment of the present invention to recycle waste energy;

Figure 15 illustrates the recovery of waste energy in hybrid coupled amplifiers according to one embodiment of the present invention;

Figure 16 illustrates a feed forward amplifier with a improved efficiency according to one embodiment of the present invention;

Figure 17 illustrates a graph of the multi-carrier transmitter efficiency according to one embodiment of the present invention;

Figure 18 illustrates a wide dynamic range rectifier circuit according to one embodiment of the present invention; and

Figure 19 illustrates a wide dynamic range rectifier based upon quarter-wave transformer.

Detailed Description of the Preferred Embodiments

An overdimensioned matrix power amplifier according to one embodiment of the present invention is illustrated in Figure 4. A set of N input signals is connected to the input ports of an M + M port butler matrix chosen according to Babcock or other optimum spacing. To apply Babcock spacing, the butler matrix ports are numbered with increasing integers according to the phase increments with which successive input signals appear combined at the outputs. For example, port 0 refers to the butler matrix output corresponding to the sum of the input signals with no phase shift. Port 1 refers to the output corresponding to the sum of input signals with an increasing phase shift in the series 0, d \( \Phi \), 2d \( \Phi \), 3d \( \Phi \) etc. Port 2 corresponds to phase shifts 0, 2d \( \Phi \), 4d \( \Phi \), 6d \( \Phi \)... etc. The M outputs of the butler matrix 40 are amplified in non-linear power amplifiers. Amplifier outputs are combined using a similar M + M port butler
matrix 44 and the N Babcock-spaced output ports yield desired amplified signals, while the remaining M - N signals are terminated to dissipate unwanted intermodulation as heat or energy in dummy loads 46.

An extreme case of the above occurs when non-linear power 5 amplifiers 42 are saturated class-C amplifiers. The output signal of a class-c amplifier is characterized only by its instantaneous phase, so the general problem can be stated as finding M phases that will result in the N arbitrary signals being approximated as closely as possible with intermodulation and distortion being directed to M-N terminated ports. This problem is solved in the present invention by realizing that to define N arbitrary output signals, 2N degrees of freedom are necessary, as the arbitrary signals have both a real and an imaginary part. Thus, if each input signal can only vary in phase, it has only one degree of freedom and 2N must be specified in order to synthesize the N arbitrary signals.

Consequently, a 2N-channel matrix power amplifier with a 2N+2N port Butler matrix combining its outputs allows N amplified output signals to be reproduced exactly at N of the output ports of the Butler matrix, with all intermodulation being collected at the other N ports which are terminated in dummy loads, providing that a method of deriving 2N phase-varying or constant-envelope signals can be found such that selected N combinations produced by the Butler matrix equate to the N desired signals.

One method is to use N configurations of constant-amplitude amplifier pairs to amplify each of the N varying-amplitude signals. Each pair of amplifiers in this arrangement is driven with a pair of constant 25 amplitude signals having a mean phase equal to that of a wanted signal and a phase difference equal to twice the ARCCOSINE of the ratio of the instantaneous desired signal amplitude to its peak amplitude. A hybrid junction can then be used to form the sum and difference of the amplifier pair's output signals, the sum having the desired phase and amplitude and the
difference being terminated in a dummy load or subjected to a waste energy
to a waste energy recovery technique which will be described further below.

Figure 5 illustrates a linear power amplifier using class-C according
to one embodiment of the present invention. A logarithmic amplifier/detector 21 can if more convenient operate at a lower, intermediate
frequency than that to be amplified by the power amplifiers. In this case, an
optional upconverting 52 consisting of a local oscillator 53, a mixer 54 and a
selective filter 55, is used to convert the intermediate frequency to the final
frequency. Otherwise, the amplifier 21 can in principle operate directly at
the final frequency and the upconverting 23 may be omitted.

The amplifier 21 is of a known type and produces a hard-limited
output signal which preserves phase information but has amplitude variations
removed. The input signal's amplitude variations are encoded by the
logarithmic amplifier's progressive detection process into a signal
proportional to the logarithm of the amplitude which, after optional low-pass
filtering in low pass filter 60, is applied to a function generator 62. The
function generator 62 converts the time-varying logamplitude signal into two
time varying signals labelled $\text{COS} \Theta$ and $\text{SIN} \Theta$ to indicate that the sum of
their squares is always unity. $\text{COS} \Theta$ is equal to the ratio of instantaneous
amplitude to peak amplitude, or, expressed in terms of logamplitudes, is the
antilog of the difference between instantaneous logamplitude and peak
logamplitude. The peak logamplitude can either be determined by the
function generator 62 over a sufficiently long period, or set from outside by
means of a "SCALE" input. The $\text{SIN} \Theta$ function is merely $\sqrt{1 - \text{COS}^2 \Theta}$.

One means of implementing such a function generator is by digitizing
LOG(A) and then using digital signal processing circuitry comprising
function look-up tables. Analog means can also be used however, employing
diode or transistor networks that synthesize a piece-wise linear
approximation to the desired functions.
In the digital implementation, the LOGAMPLITUDE signal is sampled and digitized at a rate at least equal to the total signal bandwidth. The SCALE signal is set to the peak of the LOGAMPLITUDE signal and subtracted from it to produce a value equal to the LOG of the ratio of instantaneous to peak amplitude. This value is always negative but may of course be complemented to produce a digital value that is always positive. This binary value between 000...000 and 111...111 is then used as the address to a pre-computed table of corresponding cos(θ) and sin(θ) values. The values are precomputed using the formula θ = 2\text{ARCOSINE}[\text{EXP}(\lambda A)]

where A is the address and λ is a suitable scaling value depending on the number of bits of the address and their significance is to make the resultant θ value equal to twice the ARCOSINE of the instantaneous to peak amplitude ratio. The digital cos(θ) and sin(θ) values are then converted to analog voltage waveforms using D to A convertors and low-pass filters.

The COSθ and SINθ functions are used to multiply the constant amplitude signal supplied by the logarithmic amplifier 50, the low-pass filter 51 and the upconvertor 52 if used. The multiplier 58 effectively re-applies the amplitude modulation removed by the hard limiting amplifier 50 on the upper channel while applying a complementary amplitude modulation to the lower channel such that the sum of the squares of the new amplitudes A1 and A2 is unity. This arises through choice of the functions COSθ and SINθ whose sum square is automatically unity. The new signals from the multipliers 58 are A1·EXP(jΦ) and A2·EXP(jΦ) where Φ is the phase of the original input signal. These two signals are combined using a quadrature coupler 56 at the inputs of the class-C power amplifier to produce (A1+jA2)EXP(jΦ) and (A2+jA1)EXP(jΦ). Since the sum of the squares of the real and imaginary parts of these are by design unity, the class-C power amplifiers 57 receive constant amplitude drive signals so as to operate at maximum efficiency. The entire chain of components described up to the
quadrature coupler 56 is suitable for integration on a small, low-cost silicon chip with a size of only 3mm x 3mm.

The two matched, class-C power amplifier stages 57 amplify their respective constant amplitude signals and then recombine their outputs using the second of the couplers 56. One output of the coupler 56 is $G \exp(j\Phi)$ while the other output of the coupler 56 is $G \exp(j\Phi)$ where $G$ is the amplification gain. The first output is the desired output signal which represents the original input signal and its phase and amplitude variations. The second output is a waste energy signal that is either 10 dissipated as heat in a dummy load 61 or subjected to the waste energy recovery process as will be described below. It will be appreciated that, by using the above technique, the peak power of the output signal is limited to the sum of powers of the two class-C power amplifiers 57.

According to another embodiment of the present invention, $N$ signals are defined which are the $N+N$ port Butler matrix combinations of $N$ signals to be amplified. This can be done if desired by digital signal processing using a Fast Walsh Transform. Then each of the $N$ transformed output signals is amplified by converting to a pair of constant amplitude vectors, for example, using the technique illustrated in Figure 5, that are amplified using 20 $2N$ class-C power amplifiers. The $2N$ power amplifier outputs are then combined in pairs to produce $N$ wanted signals and $N$ waste energy signals, and the $N$ wanted signals recombined using an output $N+N$ port Butler matrix. The $N$ waste energy signals may be terminated in dummy loads which dissipate unwanted intermodulation as heat, light, other 25 electromagnetic radiation, or subjected to a waste energy recovery process as will be described below.

The advantage of the above is that any signal can at the output momentarily reach a level equal to the sum of all 2N amplifier output powers if needed. This arrangement is shown in Figure 6.
N input signals are combined in an \( N+N \) port input Butler matrix 70 to produce \( N \) output signals. These are split into DRIVE and COMPLEMENTARY DRIVE signals in drive signal splitters 71 according to the above described procedure so that each signal is a constant amplitude signal. These constant amplitude signals may be amplified efficiently by the \( N \) pairs of class-C power amplifiers 72, whose outputs are then pair-wise combined in combiners 73 to produce \( N \) wanted signals and \( N \) waste energy signals. The waste energy signals are dissipated in dummy loads 74 as heat, while the \( N \) wanted signals are decombined in output Butler matrix 75 to produce the original \( N \) input signals at an amplified power level. As a result, unwanted intermodulation products are dissipated as heat, light, or other electromagnetic radiation in dummy loads 74.

The combination of pair-wise combiners 74 and the \( N+N \) port Butler matrix 75 may be recognized as a \( 2N+2N \) port combining network with \( 2N \) inputs (from the \( 2N \) class-C power amplifiers 72) and \( 2N \) outputs (of which \( N \) are terminated in dummy loads). It is in fact a partial construction of a \( 2N+2N \) port Butler matrix that has been simplified by removing stages that merely complete the recombination of waste energy signals unnecessarily. In general, the \( 2N+2N \) output combining matrix of such a device does not need to be a full Butler matrix but can be simplified to its Fast Walsh Transform equivalent through deletion of fractional phase shifters or separation into groups of smaller transforms. In general, it is desirable that at least the wanted output signals are constituted as combinations of all the power amplifier signals such that maximum flexibility exists to vary the output power of each signal up to the sum of all the powers of the power amplifiers, should that be instantaneously needed.

According to another embodiment of the present invention, the above-described process can be used to increase the output power in certain timeslots used for transmitting paging calls to mobile phones, to increase the probability of reception.
In a TDMA system, each communication signal is allocated a portion of a time-multiplex frame period, called a time slot, on a common carrier frequency. In a TDMA system, it may be desirable to have the flexibility to raise the power level in certain time slots. A higher power level can, for example, be needed to communicate with a mobile ground terminal that is temporarily suffering a signal attenuation due to buildings, trees, or some other object. A higher power level can also be desirable in the timeslots used for broadcasting paging messages to mobile terminals in order to guarantee reception while their antennas are in a stowed position.

This embodiment of the present invention comprises a multi-beam satellite antenna for dividing the area illuminated on the earth into cells. A matrix power amplifier is provided with an output corresponding to each antenna beam and comprised of a plurality of power amplifiers connected by means of Butler matrices at their outputs to provide each beam signal.

Means are also provided to TDMA-modulate to vary the power level of the drive signals on a timeslot by timeslot basis. Means are also provided to inhibit transmission on groups of unused timeslots on any TDMA signal such that available power amplifier power can during that period be taken up by increasing the drive signals in another beam. The TDMA modulation and power varying means are preferably located on the ground. A ground station comprises the necessary signal generation for each beam signal and transmits these to the satellite. Moreover, the matrix-PA input Butler matrix combiners can also preferably be located on the ground whereby the ground station produces already combined drive signals for directly driving each of the power amplifiers and these signals are transmitted to the satellite by means of coherent feeder links as disclosed in U.S. Patent Application No. 08/179,953, entitled "A Cellular/Satellite Communications System With Improved Frequency Re-use", filed January 11, 1994, which is expressly incorporated by reference.
In the case where one or two timeslots in each beam is allocated for a paging/calling channel of higher power than a traffic channel, the timeslots are deliberately staggered as between the N different outputs such that no two outputs demand high power in the same timeslot. In this way a large power increase such as a factor of ten may be achieved in one signal path at a time without drawing too much of the total available power amplifier power.

In the general formulation of the class-C matrix power amplifier, drive signals for 2N constant-amplitude power amplifier stages should be constructed in order to produce N signals with a desired amplitude and phase modulation at N of the output ports of a 2N+2N port output combining network and a further N waste energy signals at the other N output ports which may be dissipated as heat in dummy loads or subject to a waste energy recovery process which will now be disclosed with reference to Figure 7.

A completely general passive combining structure 80 combines the outputs of 2N power amplifier stages 82 to produce N wanted signals and N unwanted signals that are dissipated in dummy loads 81 as heat or light. In a satellite application, the latter can be achieved by use of incandescent filament lamps as the dummy loads, and the resultant light focused back on the solar cell array. The passive combining network can be the known prior art Butler matrix, or a reduced Butler matrix formed by omitting combining waste energy signals, or a simplified Butler matrix corresponding to a Fast Walsh Transform structure as opposed to the usual FFT structure.

The general combining structure can be represented as a 2N by 2N matrix having complex coefficients Cij. The complex coefficients Cij describe both the phase and amount of signal voltage or current transfer from power amplifier number j to output port number i. Thus the N desired output signals may be expressed as

where GAIN is the intended amplification through the device.
\[
\begin{bmatrix}
S_1 \\
S_2 \\
S_3 \\
\vdots \\
S_n
\end{bmatrix} =
\begin{bmatrix}
C_{11} & C_{12} & C_{13} & C_{14} & \ldots & C_{1,2n} \\
C_{21} & C_{22} & & & & \vdots \\
& & \ddots & & \vdots & \vdots \\
C_{(2n,1)} & \ldots & & & & C_{(2n,2n)}
\end{bmatrix}
\begin{bmatrix}
\exp(j\theta_1) \\
\exp(j\theta_2) \\
\vdots \\
\exp(j\theta_{2n})
\end{bmatrix}
\]

These equations have \(N\) complex (2N real) conditions to be satisfied (the \(N\) real and \(N\) imaginary parts of the desired signals \(S_i\)), and 2N degrees of freedom (the 2N phases \(\theta_j\)). However the non-linear nature of these equations hampers their direct solution for the phases \(j\theta\). Instead, in the present invention, the equations are differentiated to obtain a set of linear equations for the changes in phases \(\Delta\theta_j\) needed such that the desired signals \(S_i\) will change from their previous values \(S(k-1)\) to their new intended values \(S(k)\). Thus we obtain:

\[S(k)-S(k-1) = jGAIN \cdot C \cdot T \cdot dT\]

where \(C\) is shorthand notation for the coefficient matrix, and \(T\) is the diagonal matrix

\[
\begin{bmatrix}
\exp(j\theta_1) & 0 & 0 & 0 & \ldots & 0 \\
0 & \exp(j\theta_2) & 0 & 0 & \ldots & 0 \\
0 & 0 & \exp(j\theta_3) & 0 & \ldots & 0 \\
\vdots & \vdots & \vdots & \vdots & \ddots & \exp(j\theta_{2n}) \\
0 & 0 & 0 & \ldots & \exp(j\theta_{2n})
\end{bmatrix}
\]

and \(dT\) is a vector of the 2N phase changes to be found.

By denoting the product \(jGAIN \cdot C \cdot T\) by the \(N\) by 2N complex matrix \(U\), and the difference between successive signal samples \(S(k)-S(k-1)\) as \(dS\), the following equation is obtained:

\[U \cdot dT = dS\]

The \(N\) by 2N complex matrix \(U\) may be regarded as a 2N by 2N real matrix if the \(Nx2N\) real coefficients \(UR_{ij}\) are row-interleaved with the \(Nx2N\) imaginary parts \(UI_{ij}\) in the following pattern:

\[
\begin{align*}
UR_{11} & \quad UR_{12} & \quad UR_{13} & \ldots & \quad UR_{1(2n)} \\
UI_{11} & \quad UI_{12} & \quad UI_{13} & \ldots & \quad UI_{1(2n)}
\end{align*}
\]
Likewise, the N complex $d_S$ values comprise 2N real values and can be regarded as a 2N point real vector by interlacing real and imaginary parts vertically. Thus, the N complex equations $U \cdot d_T = d_S$ are actually 2N real equations that are simply solved by a real equation solving process to yield

$$d_T = U^{-1} \cdot d_S$$

The $d_T$ values so found are added to corresponding $\Theta$ values to obtain new $\Theta$ values. These can be used to calculate new values of $\text{EXP}(j\Theta)$ which are the required drive signals for the power amplifiers. This conversion of $\Theta$ values to drive signals can take place by simply applying digitized $\Theta$ values to a $\text{COS}/\text{SIN}$ look-up table or ROM to obtain values for $\text{COS}(\Theta)$ and $\text{SIN}(\Theta)$ which are the real and imaginary parts of $\text{EXP}(j\Theta)$.

The numerical values of $\text{COS}(\Theta)$ and $\text{SIN}(\Theta)$ are thenDtoA converted and used to drive a quadrature modulator to produce the radio-frequency drive signals as shown in Figure 8, which will be explained in detail below. Since modern technology is capable of realizingDtoA convertors of adequate precision (e.g. 8 bits) which can run at 1000 Megasamples per second, such a digital implementation is practically useable for all practical bandwidths.

The new $\Theta$ values and the $C$ matrix can be used to calculate the $S$-values actually achieved by the linearizing approximation of differentiation. Alternatively, the $S$-values achieved may be measured at the wanted signal outputs. Either way, it is the actually achieved values of $S$ that are used as
S(k-1) to form the differences dS with the next desired set of samples S(k).
In this way, errors do not propagate and are limited. In the case where measured S values are subtracted from the next set of desired values S(k), the system can be described as N-channel Cartesian feedback. Cartesian feedback is a known technique for reducing distortion in a quasi linear power amplifier through using a signal assessment demodulator to measure the achieved complex values of a signal at the output of a power amplifier and comparing them with desired values to produce error values. The error values are integrated and fed to a quadrature modulator to produce new values of the power amplifier drive signals that will cause the power amplifier more nearly to deliver the desired complex signal output. An advantageous method for the above is described in U.S. Patent Application No. 08/068,087, entitled "Selfadjusting Modulator", which is incorporated herein by reference. In the case of the above inventive matrix power amplifier, feeding back measured complex values of the N output signals so as better to achieve the next set of complex values is a form of Cartesian feedback for correcting signal matrices instead of single complex signal values.

By determining the new dS values in the above-described manner, the new θ values are used with the C matrix to determine the new U matrix. A simplified way to perform this function is to note that the effect of adding Dθ1 to Dθ2 will be to rotate the previous values of U1j through an angle Dθ1, which causes a transfer of a fraction of their imaginary parts to their real parts and vice versa. For small values of Dθ, this allows the U matrix to be updated with no multiplies. The Dθ values can always be kept small by choosing successive sample values S(k-1), S(k), S(k+1) ... to be sufficiently closely spaced in time. A high speed digital logic machine or computer may be envisaged for performing these calculations in real time to give continuous drive waveforms to the power amplifier stages of several MHz bandwidth. For a satellite application, such a machine is preferably
located on the ground and the resulting drive waveforms only communicated to the satellite via 2N mutually coherent feeder links as disclosed in U.S. Patent Application No. 08/179,953, entitled "A Cellular/Satellite Communications System With Improved Frequency Re-use", filed January 11, 1994, which is expressly incorporated herein by reference.

The arrangement for calculating the phase signals is illustrated in Figure 8. A difference calculator 100 computes the difference between the last approximation to the desired signals at instant k-1 and the new signal samples Si at instant k. The N complex differences are input to a matrix computer 102 that multiplies them by an inverse U-matrix to obtain 2N delta-phase values. The delta phase values are accumulated in 2N phase accumulators 204 to produce 2N Θ values that are converted to COSINE and SINE values using COS/SIN ROMs 106 and thenDtoA converted using digital to analog convertors 108. The resulting 2N I,Q signals are passed to 2N quadrature modulators that impress the signals on the desired radio carrier frequency to obtain the signals EXP(jΘ) indicate in Figure 7 for amplification by the constant amplitude power amplifiers.

A simplified alternative exists when the signals to be communicated Si are radio signals modulated with digital information streams. If the information streams on each of the signal paths are symbol or bit synchronous, then the waveforms Si at any instant depend on a limited number of past and future bits according to the smearing produced by the impulse response of the premodulation filtering. In the limit, an S-value in the center of a symbol at least may depend only on that symbol. With binary signalling, the symbol can only take on one of two values, 0 or 1, corresponding to an Si of +1 or -1 with suitable scaling to the desired output power and frequency. For a matrix power amplifier of limited size, for example 16 channels, this means that there can only be \(2^4 = 65536\) different vectors S when sampled mid-bit. The 2N values of Θ corresponding to each of these S vectors can be precomputed and stored in a
reasonably sized ROM, and may be retrieved when needed by applying the current 16-bits from the 16 channels as an address. For practical purposes, adequate shaping of the data transitions from one bit period to the next in order to control the spectrum may be obtainable by smoothly transitioning between these sets of \( \Theta \) values by means of interpolation. Thus, if a particular \( \Theta \) value for a current set of 16 bits being transmitted was 130 degrees and a next value was -170 degrees, the \( \Theta \) value would be moved from the old value to the new by means of the sequence 135, 140, 145, 150, 155, 160, 165, 170, 175, 180, -175, -170 noting that the shortest path is taken. A \( \Theta \) value that had less far to move would take the same number of smaller steps. At each step, the values of \text{THETA} \) would be applied via \text{COS/SIN ROMs} and \text{DtoA convertors} to a quadrature modulator in order to convert them to the desired radio-frequency drive signals for the power amplifiers.

The general principle of the present invention for obtaining multi-channel linear signal amplification using non-linear and even saturating power amplifier stages has now been explained together with a number of implementations. The aim of the present invention, to reduce the transmission of unwanted intermodulation signals produced by the power amplifier non-linearities, is achieved through choice of drive signals in a coupled power amplifier arrangement such that unwanted intermodulation is directed to an output not used for wanted signal transmission, where the unwanted energy can be dissipated as heat or light in a dummy load, or subject to a waste energy recovery procedure.

In another embodiment of the present invention, the amplifier outputs are not combined before being fed to a multi-beam antenna but rather are fed directly to the elements of an antenna array. Figure 9 illustrates the use of a cylindrical array of slot antennas as might be used for a phased array base station as disclosed in U.S. Patent Application No. 08/179,953, entitled "A

Cellular/Satellite Communications System With Improved Frequency Re-
use", which is incorporated herein by reference above. In such a phased array, a number of antenna elements, such as 8 horizontal columns around the cylinder and 20 vertical columns, are used for transmission or reception of signals from mobile radio telephones. For transmission, the elements in each of the vertical columns may be driven in phase from the output of a single power amplifier by use of a 20-way, passive power-splitter. Alternatively, each element may be equipped with its own associated smaller power amplifier (of 1/20th the output power) and the 20 amplifiers in each column are driven in phase using the same drive signal.

Each column thus produces radiation focussed in the vertical plane but still spread over a fairly wide azimuth. When the radiation from all eight columns is evaluated however, by appropriate choice of relative amplitude and phase between the eight columns, focussing in the azimuthal plane is also produced thereby narrowing the horizontal radiation pattern and increasing the directivity gain.

When either of the above arrangements is used for transmitting multiple signals each in a different desired direction, the signal for each column comprises the sum of the different signals with an appropriate set of amplitude and phase (complex) weightings for that column. For example, the signals $S_1, S_2, S_3 \ldots$ for the eight columns may be formed from the signals $T_1, T_2, T_3$ to be transmitted as follows:

$$S_1 = 0.5jT_1 + (0.7+0.1j)T_2$$
$$S_2 = T_1 + (0.6+0.3j)T_2 + 0.5jT_3$$
$$S_3 = 0.5jT_1 + (0.1+0.4j)T_2 + T_3 + (0.1+0.6j)T_4$$
$$S_4 = (-0.1-0.2j)T_2 + 0.5jT_3 + (0.9-0.1j)T_4 \ldots$$

etc., where $j = \sqrt{-1}$ signifying a 90-degree phase-changed component.

It can be seen that the signal $S_i$ to be amplified for application to a column of elements comprises the complex-weighted sum of the independent signals $T_1, T_2$ etc. Thus, the amplifier or amplifiers for that column have to faithfully reproduce not just a single signal (that could have been a constant amplitude signal as with analog FM) but the sum of independent signals that
is not a constant amplitude signal. Thus, in prior art phased array base stations, the use of linear amplifiers that reproduced both the amplitude and phase variations of the composite drive signals is required. In U.S. Patent No. 3,917,998 to Welti, the use of a coupled matrix of power amplifiers is disclosed with the property that no single amplifier necessarily has to generate the peak power that any one antenna element or feed may require; however the possibility of using constant-amplitude power amplifiers was not disclosed. In a previous embodiment of the present invention, the possibility of using class-C or constant amplitude power amplifiers in a coupled matrix is disclosed, through overdimensioning the matrix by a factor of two at least relative to the number of independently-specifiable amplified output signals desired. The previous embodiment consisted of a number at least $2N$ of class-C power amplifiers coupled at their outputs by an at least $2N+2N$ port Butler matrix or lossless coupling network, wherein the $2N$ input ports being connected to said amplifier outputs and $N$ of said coupling network output ports being said desired amplified signal outputs, the rest being terminated in dummy loads. As a result, the unwanted intermodulation products are dissipated in the dummy loads as heat.

In the present embodiment of the present invention, the $2N+2N$ Butler matrix is not needed. Instead, each column of elements in the array is split into even and odd elements numbered vertically from 1 at the top to at least $2N$ at the bottom. In one implementation of this embodiment, elements 1,3,5 etc. of a column are connected by a passive $N$-way power splitter driven by a first power amplifier, while elements 2,4,6,8 ... are connected by a second $N$-way power splitter driven by a second power amplifier. In a second implementation of the present embodiment, each element is equipped with a smaller power amplifier and the amplifiers attached to even elements are all driven with a first drive signal while amplifiers attached to odd elements are all driven with a second drive signal.

If the drive signals are the same, radiation from the even and odd elements
will reinforce in the horizontal plane, while if the drive signals are in antiphase, there will be no radiation in the horizontal plane. Thus it is possible by varying the relative phasing between in phase and antiphase to produce varying amplitudes of signal radiation in the horizontal plane even though the individual elements of the column receive constant amplitude signals from their respective power amplifiers.

For the present invention, the inventive cellular base station comprises at least one but preferably a number of such columns of vertically interlaced elements disposed with cylindric symmetry around 360 degrees of azimuth on top of an antenna tower or mast. The angular spacing of the columns is chosen principally to avoid mechanical interference between them, but may be greater than this minimum spacing if this gives the array greater horizontal directivity. As will be described below, each column of elements must be fed with two signals, to the even and odd amplifiers respectively, such that the net horizontal radiation will equate to the desired composite signals $S_i$ defined above.

If signal $S_i$ to be radiated by column $i$ is expressed as a time-varying amplitude $A(t)$ and a time varying phase $\phi(t)$, then let

$$D_1 = A_0 \cdot \exp \{ j(\phi + \theta) \}$$
$$D_2 = A_0 \cdot \exp \{ j(\phi - \theta) \}$$

be the time varying drive signals for the even and odd elements of column $i$,

where

$$\cos(\theta) = A(t)/2A_0$$

It may be verified that, when $D_1$ and $D_2$ are added to calculate the radiation in the horizontal plane, we obtain

$$D_1 + D_2 = A_0 \cdot [\exp \{ j(\phi - \theta) \} + \exp \{ j(\phi + \theta) \}]$$
$$= A_0 \cdot [\exp \{ j\phi \} + \exp \{ -j\theta \}] \cdot \exp \{ j\phi \}$$
$$= 2A_0 \cdot \cos(\theta) \cdot \exp \{ j\phi \}$$
$$= 2A_0 \cdot (A(t)/2A_0) \cdot \exp \{ j\phi \}$$
$$= A(t) \cdot \exp \{ j\phi \}, \text{ as desired.}$$
The principle of the present embodiment of the present invention may be extended by dividing a column of elements into four equal groups, i.e., nos. 1,5,9 ... 2,6,10... 3,7,11 ... 4,8,12 and so on. Each group is connected to a single power amplifier for that group by means of a power splitter, or each element is equipped with its own power amplifier and the amplifiers of a group are driven in phase with a drive signal adapted for each group. Then, a set of four drive signals is found such that desired signal radiation occurs at up to two desired elevation angles, which may if desired both be in the horizontal plane. In general, the problem of how to produce radiation of N desired signals at N desired angles of elevation from a column of at least 2N constant-amplitude radiating elements may be solved by a similar mathematical process to that described above for generating N desired signals of varying amplitude and phase using at least 2N signals of constant amplitude and varying phase.

Thus, it has been shown above how each column of elements in a cylindrical array may be arranged to produce a desired contribution to radiation at a specified angle of elevation, e.g., in the horizontal plane. It remains to be explained how the different contributions from each column are chosen so as to focus the resultant radiation also to desired angles of azimuth. This is done simply by arranging the radiation from the columns to have the complex conjugate relationship to each other compared to the signals that would be received from the desired azimuth. For example, if column 1 would receive from a mobile transmitter lying at 0 degrees of azimuth a signal of amplitude 0.5 and phase 120 degrees while column 2 would receive a signal of 0.7 and phase 50 degrees, that is amplitudes in the ratio 0.5:0.7 and phases differing by -70 degrees, then column 1 and column 2 should produce radiation contributions in the same amplitude ratio 0.5:0.7 for transmission but with a relative phase of +70 degrees.

The amplitude and phase relationship of the array elements for reception can be predicted from the theoretical or measured polar patterns of
the constituent elements and their physical disposition in the array. Thus, the relative phases and amplitudes for transmission in any direction can be predetermined by changing the signs of the phases. It is often sufficient to quantize the number of possible directions the array can be called upon to transmit in to a limited number of beams spaced, for example, at 5 degree intervals around 360 degrees of azimuth. The phase relationships and amplitude ratios can thus be precomputed for each of these 72 directions. If the array is formed by 8 columns of elements, there exists furthermore an 8-fold symmetry such that said 72 possible phase and amplitude relationships reduce to only 9 distinct patterns that are repeated by shifting the whole pattern in steps of one column around the array. It is thus a relatively straightforward process to store these 9 patterns in a signal processor and to select the pattern and the shift needed to radiate a given signal in a given direction to the nearest 5 degrees. When this has been done for all signals desired to be radiated, and the results summed to determine the composite radiation to be produced by each column of elements, the drive signals for the constant-amplitude amplifiers associated with each column are generated using the method described above.

Figure 10 illustrates a block diagram of a transmit signal processor designed to accomplish the above-described process. A set of signals to be transmitted T1,T2 ... Tn along with associated direction information Θ1,Θ2 ... is applied to transmit matrix processor 110. Signals T1,T2 etc. are preferably in the form of a digitized sample stream produced by other signal processor(s) (not shown) that can include speech coding, error correction coding and digital conversion to modulated radio signal form. The latter represents each signal as a stream of complex numerical samples having a real and an imaginary part or alternatively in polar form using a phase and amplitude. The matrix processor 110 uses the direction information Θ1, Θ2 etc. to select or compute a set of complex weighting coefficients using stored data in a memory 112 which is adapted to the array configuration. In its
simplest form, direction information \( \Theta_1, \Theta_2 \) etc. can consist of a beam number, and the beam number is used to select a set of precomputed stored coefficients from the memory 112. The coefficients are used in complex multiplication with signals \( T_1, T_2 \) to produce weighted sums \( S_1, S_2 \) ... etc.

5 The complex weighting coefficients are calculated for each signal according to its desired direction of radiation and using the principle of phase-conjugating the signals that would be received from the desired direction, as disclosed above. The weighting coefficients may also be calculated such as to minimize the transmit power consumed to produce a given signal strength at the receivers, as disclosed in the incorporated U.S. Patent Application No. 08/179,953, entitled "A Cellular/Satellite Communications System With Improved Frequency Re-use".

The number of sum signals produced is equal to the number of columns of array elements, which may be greater than or less than the number of signals to be transmitted. Of course, signals to be transmitted in the same direction at the same time are preferably modulated on different frequencies so that the same frequency is not used in the same beam number more than once, except in a CDMA context. The frequencies of each signal are reflected in the nature of the modulated signals \( T_1 \). Alternatively, the signals \( T_1 \) can be nominally represented on a zero-frequency carrier and the correct desired relative frequency applied within the matrix processor 110 by including a phase slope during a process of upsampling.

The composite output signals now represent the sum of signals at different frequencies and thus are wide band signals with a commensurately increased sample rate. Each signal \( S_i \) is then converted in drive signal splitters 114 to a pair of constant amplitude signals whose sum has the desired instantaneous phase and amplitude of \( S_i \). This process of drive splitting is preferably still performed in the digital signal domain, but shortly thereafter it is appropriate to convert said drive signals to analog form with the aid of DTOA converters. Since the numerical form consists of complex
numbers, one convertor may be used for the real part and another for the imaginary part. The two signals produced are termed in the known art as I, Q signals and may be applied to a known quadrature modulator device to translate them to a desired radio frequency band. Translated signals are then amplified to a transmit power level using efficient, constant-amplitude power amplifiers 116 and 118 for even and odd column elements respectively. These amplifiers may be distributed among the array elements themselves.

It will be appreciated that the present invention may be applied similarly to arrays of elements disposed on a cylindrical surface, a planar surface, or any other surface. The general principle is to provide a superfluity of elements of preferably at least a factor of two over and above the number of distinctly different signal directions the array is desired to resolve. In this way, the array when transmitting can comprise efficient constant-amplitude power amplifiers and unwanted signal intermodulation products that arise can be arranged to be radiated in directions other than those in which the array radiates wanted signal energy. For example, an orbiting satellite carrying such an array can be arranged to irradiate the earth with wanted signals at different locations while intermodulation products (unwanted signals) are radiated harmlessly into space. In this application, the invention disclosed in the incorporated U.S. Patent Application No. 08/179,953, entitled "A Cellular/Satellite Communications System With Improved Frequency Re-use", may be employed to place the generation of the drive signals for said array elements and associated amplifiers on the ground, the resulting signals being conveyed to the satellite using coherent feeder links from a ground-based hub-station. An advantage of the present invention is a reduction of the heat that would normally have to be dissipated in a less efficient, linear power amplifier designed not to produce such unwanted intermodulation signals.

Another embodiment of the present invention relates to communications systems using relay stations and in particular to systems
where the relay station is an earth-orbiting satellite having a communications transponder. The communications transponder receives signals broadcast from a first ground station in a first frequency band called the forward feeder link and translates them to a second frequency band called the downlink for relaying to a second ground-based station, which may be a small handportable station. The transponder is furthermore equipped with a multiplicity of such channels each having a transmit power amplifier and connected to a multiple beam antenna. The invention employs a combining network such as a Butler Matrix to connect the multiplicity of power amplifiers to the multiple beam antenna such that each amplifier amplifies a part of every desired beam signal instead of each amplifier being dedicated to amplify only a single desired beam signal.

In contrast with the prior art, an inverse Butler combining device is employed at the first ground station in order to form weighted sums of the desired beam signals for transponding using the power amplifiers. This has two advantages over the prior art method of locating the inverse Butler matrix in the satellite; firstly, dynamic reallocation of power between antenna beams may be accomplished without large variations in the corresponding forward feeder link signals; secondly, pre-distortion of signals sent on the forward feeder links may be used to partially compensate for distortion in associated transponder channel power amplifiers.

Additional advantages are provided in the preferred implementation through use of a greater number of forward feeder links and corresponding transponder channels and power amplifiers than the number of antenna beams, thus providing a degree of redundancy against failures. The latter also allows distortion products to be directed towards the unused Butler matrix output ports that are terminated in dummy loads and not connected to antenna beams.

The ability to radiate heat from an orbiting satellite can often be the dominant factor in limiting the capacity of a satellite communications system.
Satellite communications systems designed to provide communication with a large number of mobile stations are of so-called multiple access type and may employ Frequency Division Multiple Access, Time-Division Multiple Access, Code Division Multiple Access, or any combination of these techniques. In FDMA or CDMA systems, a large number of signals must be radiated simultaneously leading to the problem of intermodulation in transmitters. In TDMA signals, a frame period is divided into timeslots, and each signal occupies a timeslot. Thus, in a pure TDMA system, it is not necessary to radiated many signals simultaneously, and efficient constant amplitude transmitters can be used. In practice, however, lack of available frequency spectrum requires that a fourth multiple access method also be employed, called Space Division Multiple Access (SDMA) or "Frequency Re-use". Frequency Re-use is the well-known cellular radio-telephone technique of dividing the earth into cells and permitting cells that are sufficiently separated to employ the same frequencies. Thus, even when a satellite system employs pure TDMA within each cell, it may have to employ SDMA to permit other cells to use the same frequency; thus the satellite ends up having to radiate several signals at the same time in different directions. The invention described above may be employed to allow a phased array of antenna elements with associated efficient, class-C power amplifiers to generate a number of TDMA signals for radiation instantaneously in different directions. The set of directions may change from one timeslot to the next as disclosed in U.S. Patent Application No. 08/179,953, entitled "A Cellular/Satellite Communications System With Improved Frequency Re-use". The overall efficiency of such an inventive arrangement expressed in terms of conversion of DC power from a solar array or battery into usefully radiated signal energy may be no greater than if a prior art arrangement using linear amplifiers had been employed. However, the inefficiency shows up less in terms of heat dissipation, and instead as the radiation of radio energy in the form of intermodulation
products harmlessly into space. Alternatively, the intermodulation may be subject to the waste energy recovery procedure herein described.

TDMA is a preferred choice for such a transponder as a communications system is often less than 100% loaded. In the TDMA case, the inventive transponder is run at maximum efficiency for active timeslots and switched off for timeslots not presently used. To accomplish this, traffic is preferably sorted so as to occupy as far as possible the same active timeslots on all beams, which ensures that the same timeslots are inactive on every beam. The entire transponder array may then be powered down for timeslots that are inactive on all beams. For timeslots that are inactive on many but not all beams, it may be efficient to power-down certain array elements only and arrange that the others are driven to maximum output to support the other beams, thus reducing heat dissipation to a minimum.

In its simplest form, this advantage of the current invention may be obtained using the arrangement of Figure 11. A pair of efficient, constant-amplitude power amplifiers 122 and 124 amplify signals produced either by drive splitter 120 or separately received from the ground via two coherent feeder links. A hybrid junction 126 combines the output signals from the power amplifiers to produce a sum signal and a difference signal. The drive signals may be arranged such that either the sum or difference signal is the desired signal. In Figure 11, the sum signal is desired and is connected to an antenna 130 such as a horn that illuminates the desired target, i.e., the earth. The difference signal then contains unwanted intermodulation products. In prior art systems, the difference signal has been dissipated in a dummy load as heat. However, the present invention provides maximum reduction of heat by instead radiating the waste energy into space by use of a separate directional antenna 128 pointed away from the earth. The simplest form of the invention may of course be extended in an obvious manner to multiple channel transponders having many beams pointed towards the earth and waste energy dissipating beams pointed away from the earth.
Alternatively, the difference signal can be rectified using the inventive rectifier of Figures 18 or 19 and the waste energy recycled to the battery. All such arrangements are considered to be within the spirit and scope of the invention as described by the following claims.

Another embodiment of the present invention relates to recycling waste energy generated in a power amplifier. In Figure 12, a power amplifier 140 is coupled through an isolator/circulator 141 and an optional transmit filter 142 to an antenna 143. In duplex systems requiring simultaneous transmission and reception on different frequencies, the transmit filter may form part of the antenna duplex filter, the other part of the filter 144 being associated with the receiver. In non-duplexing systems such as Time Division Duplex / Time Division Multiple Access systems or simply press-to-talk systems, there may be no duplex filter but rather a transmit/receive antenna switch. The present invention is applicable to both of these configurations. In the present invention, the dummy load normally connected to the reflected power port of a circulator is replaced by a rectifier 145. The rectifier 145 converts AC radio frequency energy into a direct current which is then fed back to the battery or power source that powers the transmitter. If the efficiency of the transmitter is E1 and the efficiency of the rectifier is E2, then a fraction E1·E2 of the total energy will be recovered in the case where the antenna is a complete mismatch, reflecting all the transmitted power fed to it. The fraction E1·E2 can of course never be greater than unity. In the case where the antenna reflects a fraction R of the power fed to it, the net consumption of energy will be reduced by the factor 1-R·E1·E2. For example, if R=10%, E1=55%, and E2=70%, the battery consumption is reduced by 3.85%, which is a significant amount of savings. When the effective energy is calculated as the ratio of the power actually radiated from the antenna to the net power consumption, the efficiency curves with and without the use of the present invention are plotted in Figure 13. Figure 13 shows that the effective efficiency is less
sensitive to antenna mismatch when the present invention is used. Figure 14 illustrates the percentage of increased talk-time by using the present invention, as a function of the percentage of energy reflected by the antenna.

Another embodiment of the present invention is illustrated in Figure 15. Two similar power amplifier stages 150 and 152 are combined using a 3dB directional coupler 154 in order to obtain the sum of their output powers at the antenna 156. An unwanted difference signal is produced which, instead of being dissipated in a dummy load as in Figure 2, is converted to a DC current in rectifier 158 and the current is fed back to the battery or power source feeding the amplifiers. The same curves illustrated in Figures 13 and 14 apply to this embodiment as well.

Another embodiment of the present invention is illustrated in connection with feedforward linearization of power amplifiers. Feedforward linearization is used to improve the linearity over that achievable with simple amplifiers, or in order to obtain improved efficiency for a given linearity. An improved efficiency feedforward amplifier is illustrated in Figure 16 wherein the main amplifier 160 can be a class C amplifier generating a constant amplitude signal. When a higher amplitude is momentarily needed, an error amplifier 162 produces an output signal that adds to the output signal of the class C amplifier 160 in directional coupler 164. When a low amplitude is momentarily desired, the phase of the error signal is reversed, causing the error signal to be subtracted from the main output 166 in the directional coupler 164, while increasing the level of the difference signal 168. Normally, the energy in the difference signal will be dissipated in a dummy load and wasted. However, the present invention uses a rectifier 170 to convert the difference signal to a DC current which is fed back to the battery, thus recovering the energy. The size of the error amplifier 162 in relation to the main amplifier 160 and the choice of the coupling ratio of the directional coupler 164 for maximum overall efficiency must be made with the knowledge of the signal amplitude statistics.
Without the present invention, the efficiency is given by:

\[
Eff1 = \frac{(1-k^2)A^2+B^2}{A^2/Ec+(1-k^2)B\cdot Bpk/(k^2\cdot EL)}
\]

where \(k\) is the voltage coupling factor of the directional coupler 164,
\(Ec\) is the efficiency of the amplifier 160,
\(EL\) is the efficiency of the amplifier 162 at its maximum output amplitude \(Bpk\),
\(A\) is the constant signal amplitude produced by the amplifier 160,
\(B\) is the difference between \(A\) and the desired output signal waveform that must be contributed by amplifier 162,
\(Bpk\) is the peak amplitude of signal waveform \(B\),
and overlining signifies mean value over time.

When using the present invention, the effective efficiency is given by:

\[
Eff1 = \frac{(1-k^2)A^2+B^2}{A^2/Ec+(1-k^2)B\cdot Bpk/(k^2\cdot EL) - R\cdot D^2}
\]

where \(R\) is the rectifier efficiency and \(D\) is the difference signal given by

\[
D = k(A+B) - B/k
\]

Another embodiment of the present invention relates to recovering waste energy in high power base station transmitters for multiple carrier operation. When a cellular base station is required to support multiple conversations with mobile stations on different frequencies, the first choice for the transmitter design is between a single, high-power multi-carrier power amplifier and a multiplicity of lower power single carrier amplifiers. The multi-carrier amplifier must be linear and is very inefficient because of the high peak to mean ratio of the composite, multi-carrier signal. In the case where feedforward linearization is used, the present invention can be employed to recover waste energy from the difference port of an output coupler.
If the single carrier amplifier approach is selected, means must be provided to connect the plurality of amplifiers to the antenna. Multiple antennas are not favorable because they tend to be large, expensive and need more real estate. One way to couple multiple amplifiers to the antenna is to use a multicoupling filter, which uses frequency selectivity to isolate the different amplifiers from one another. Multicoupling filters are large, and expensive and are only feasible when the frequency difference between the multiple carriers is not too small. The alternative is to use dissipative combining, in which amplifiers may be combined in pairs using hybrid couplers or directional couplers, which are essentially sum and difference networks. Using dissipative combining for two signals, for example, a power amplifier of power 2P is used for a first signal and a second power amplifier of output power 2P for a second signal. The outputs of the two power amplifiers are then combined using a 3dB coupler. The coupler allows half of the power of each power amplifier, i.e., P from each power amplifier, to reach the antenna while the other half is normally dissipated in a dummy load. In general, dissipative combining of N signals requires that each signal be amplified to a power N times the desired power P, so that the total power of all N amplifiers is N x NP, while only NP (P from each amplifier) reaches the antenna. Where N is a power of 2, the dissipative combiner is a binary tree which combines pairs of signals and then pairs of pairs and so on to the final output. Each pair-combining network may be a 3dB coupler.

At each coupler, half of the power is extracted in a sum signal and passed to the next coupler or to the final output, while the other half is normally wasted in a dummy load. Thus, half the total power is wasted in combining two carriers, 3/4 of the total power is wasted in combining four carriers, and in general a fraction (N-1)/N of the total power is wasted when N carriers are combined. By employing the current invention, this normally wasted power is recovered at least to the extent of the rectifier efficiency R.
Thus, instead of the net efficiency being only $E/N$ where $E$ is the efficiency of one single carrier power amplifier, the effective efficiency becomes $E/(N-(N-1)E-R)$. For example, when $E=60\%$ and $R=70\%$, the effective efficiency is plotted versus $N$ in Figure 17 with and without the present invention. The figure illustrates that efficiency can be improved by a factor of more than 1.5 by using the present invention.

In multicarrier transmitters it is generally desired to minimize the production of unwanted frequency components caused by intermodulation between the carrier frequencies. These components appear at frequencies such as $2f_1-f_2$ or $2f_2-f_1$ if the hybrid couplers do not perfectly isolate the transmitter on $f_1$ from the transmitter on $f_2$. However, the inclusion of a rectifier on the difference port of the coupler can, if no care is taken, greatly contribute to the generation of intermodulation components. This phenomenon is related to the more general problem of how to produce a rectifier that transfers energy from a variable voltage AC source to a fixed DC voltage. Of course, a solution that can be used is to incorporate a regulator, preferably a pulse width modulation type, i.e., switched-mode type, between the variable DC output of the rectifier and the fixed voltage to which it is to be connected. However, an alternative and novel solution is disclosed below which employs no active circuitry.

Figure 18 illustrates a wide dynamic range rectifying circuit with a cascade of diode rectifier stages, each stage being composed of a quadrature coupler driving a pair of identical diode rectifiers, and preferably full wave rectifiers. A quadrature coupler has the property that when terminated with two identical load impedances, any energy reflected from a load impedance mismatch is output to the so-called isolated port and not returned to the source. The AC load impedance presented by each full-wave rectifier is in fact equal to the DC load impedance, which in turn is equal to the output voltage, i.e., the fixed supply voltage to which the rectified energy is to be recycled, divided by the rectified current. Because the rectified current
varies with the AC signal amplitude while the output voltage is constrained to a fixed value, the rectifier presents a variable load impedance which is not therefore matched to the source, which causes inefficiency and intermodulation. However, in the novel configuration illustrated in Figure 5 18, the power reflected when the rectifier load deviates from a perfect match is transferred to the isolated port and not returned to the source. As a result, this energy has a second chance to be recovered in the second rectifier stage, and so on. By designing each rectifier stage to be efficient at the level of residual power passed to it from a preceding stage, the net reflection effect of the cascade of rectifiers is the product of that of the individual stages, ensuring that at all source power levels in question, little energy is reflected and that the great majority is rectified and transferred to the fixed voltage level. This novel rectifier circuit thus adapts a variable voltage AC source to a fixed DC voltage without the use of active regulators.

Other constructions of such rectifiers can also be designed. For example, another embodiment of the present invention is illustrated in Figure 19. A first rectifier stage 200 is connected via a quarter wave matching transformer 202 to the near end of a transmission line 204 and is matched to the source impedance. This first rectifier is adapted by choice of matching transformer 202 efficiently to rectify small signals. For larger signals, the rectifier presents a reduced impedance which, at the junction of 202 and 204, translates into an increased impedance by virtue of the reciprocal impedance transformation performed by a quarter wave transformer. Therefore, at larger signal levels, the first rectifier does not load the transmission line 204 as much. A second rectifier stage 206 is connected via a second quarter wave matching transformer 208 to a point 1/4 wavelength downstream on the transmission line 204. This second rectifier is adapted to be below the threshold of rectification for the small signal levels for which the first rectifier is adapted. Thus, it presents a high impedance to the second quarter wave matching transformer 208 which translates to a low impedance
at the junction of 208 and 204. One quarter wavelength nearer the source at
the junction of 204 and 202, this translates to a high impedance again, thus
not loading rectifier 200. Consequently, source energy is primarily absorbed
by rectifier 200 at small signal levels and primarily by rectifier 206 at large
signal levels. The principle may be extended by the addition of further
rectifiers with associated matching transformers progressively at 1/4
wavelength increments down transmission line 204 in order to produce a
rectifier device that converts energy from an AC source of any voltage level
to a fixed DC voltage. A person ordinarily skilled in the art will also
recognize that discrete component equivalents of the disclosed transmission
line or coupler networks can be built, as well as waveguide circuits or
circuits employing circulators in order to achieve the same goal, and all such
constructions which achieve adaptation of a variable voltage AC source to a
fixed DC voltage level are considered to fall within the scope of the relevant
invention.

It will be appreciated by those of ordinary skill in the art that the
present invention can be embodied in other specific forms without
department from the spirit or essential character thereof. The presently
disclosed embodiments are therefore considered in all respects to be
illustrative and not restrictive. The scope of the invention is indicated by the
appended claims rather than the foregoing description, and all changes which
come within the meaning and range of equivalence thereof are intended to be
embraced therein.
CLAIMS:

1. An amplifying apparatus for linearly amplifying input signals to desired power levels, comprising:
   means for combining a first plurality of input signals and producing said first plurality of output signals which are combinations of input signals;
   a second plurality of coupled, non-linear power amplifier stages for amplifying said combinations of the input signals, wherein the second plurality is larger than the first plurality; and
   second means for combining said amplified combinations of the input signals, said second combining means outputing a first plurality of wanted output signals and a third plurality of unwanted signals, wherein the third plurality is the difference between the second plurality and the first plurality.

2. The amplifying apparatus according to claim 1, wherein said coupled power amplifier stages are coupled at their outputs by a passive, lossless network having said second number of inputs coupled to said amplifier outputs and said first number of wanted signal outputs and the third plurality of outputs connected to waste energy dissipating means.

3. The amplifying apparatus according to claim 2 in which said waste energy dissipating means is a dummy load or light bulb.

4. An amplifying apparatus for linearly amplifying a desired signal using a pair of coupled non-linear amplifiers, comprising:
   limiting means for separating amplitude variations from said desired signal and producing a constant amplitude signal bearing the phase of said desired signal and an amplitude-related signal;
   drive signal generation means for producing two drive signals each dependent on said constant amplitude signal and said amplitude-related
signal such that the drive signals depend on the phase of said desired signal and such that the sum of the squares of the amplitudes of said drive signals is constant; and

coupling means for coupling said two drive signals to produce two constant amplitude signals for driving said pair of non-linear power amplifiers and for coupling the outputs of said power amplifiers to produce two amplified outputs signals, one of which is said linearly amplified desired signal and the other of which is a waste energy signal.

5. The amplifying apparatus according to claim 4, wherein said waste energy signal is disposed of in dissipating means such that it does not corrupt said desired signal output.

6. The amplifying apparatus according to claim 4, wherein said limiting means is a logarithmic amplifier-detector using successive saturation and successive detection to produce a saturated output and a logamplitude signal.

7. The amplifying apparatus according to claim 6, wherein said logamplitude signal is processed to produce two amplitude signals the sum of whose squares is constant.

8. The amplifying apparatus according to claim 6, further comprising:

a filter means for removing harmonics from said saturated output signal to produce a filtered signal.

9. The amplifying means according to claim 7, wherein said harmonic-filtered signal is upconverted to a desired output frequency using
local oscillator means, heterodyne mixing means and filtering means to select a desired mixer output frequency.

10. The amplifying apparatus according to claim 7, wherein said filtered signal is multiplied by said two amplitude signals in separate multipliers.

11. The amplifying apparatus according to claim 7, wherein said upconverted signal is multiplied by said two amplitude signals using separate multipliers.

12. The amplifying apparatus according to claim 7, wherein said saturated output is a square wave signal and is multiplied by said two amplitude signals to produce two multiplied square wave signals that are subsequently low-pass filtered.

13. The amplifying apparatus according to claim 4 used in a multi-channel amplifier further comprising:
input coupling means having a first plurality of inputs for signals to be amplified and the first plurality of outputs for driving said amplifying apparatus;
a separate one of said amplifying apparatus connected to each of said outputs of said input coupling means;
output coupling means connected to the outputs of each of said separate amplifying apparatus and producing a second plurality of coupled outputs corresponding to said amplified desired signals.

14. The amplifying apparatus according to claim 13, wherein said waste energy signals are dissipated in dissipating means so as not to corrupt said desired signal outputs.
15. A matrix power amplifier apparatus for amplifying a first plurality of signals varying in amplitude and/or phase to desired amplified power levels using a second plurality of constant-envelope power amplifier stages, said second plurality being equal to at least twice said first plurality, comprising:

   passive lossless combining means for combining the outputs of said second plurality of power amplifier stages to produce said first plurality of output signals and a third plurality of waste energy signals; and signal generator means for generating said second plurality of phase varying signals of constant amplitude in dependence on said first plurality of signals such that said first plurality of output signals are equal to said desired amplified signals at said desired power levels.

16. The matrix power amplifier according to claim 15, wherein said signal generator comprises:

   phase computing means to calculate said second plurality of phase values in dependence on said first plurality of signals;
   COS/SIN means and digital to analog conversion means to convert said phase values to a corresponding number of I,Q signal pairs; and multiple quadrature modulator means to modulate said I,Q signal pairs on to a desired radio frequency carrier for amplification by said power amplifier stages.

17. The matrix power amplifier according to claim 16, wherein said phase computer operates in dependence on the difference between new input signal samples and an approximation to previous signal samples.

18. The matrix power amplifier according to claim 17, wherein said approximation to previous signal samples includes measurements made on the output signals of said matrix power amplifier.
19. The matrix power amplifier according to claim 18, wherein said measurements are carried out using quadrature demodulators.

20. An amplifying apparatus for linearly amplifying a number of input signals to produce corresponding amplified outputs using a number of coupled non-linear power amplifiers, comprising:

input combining means for combining said input signals to produce a first plurality of combined signals for amplification;
multi-channel Cartesian feedback means for processing said amplified output signals to produce the first plurality of feedback signals;
multi-channel comparator means for comparing said input signals with said feedback signals to produce the first plurality of error signals and filtering them;
output combining means for combining the outputs of said non-linear amplifiers to produce a second plurality of combined output signals;
multi-channel quadrature modulator means to convert said filtered error signals to drive signals for said non-linear amplifiers such that a selected first plurality of said combined output signals correspond to said desired amplified input signals and any remaining are waste energy signals.

21. The amplifying apparatus of claim 20, wherein said number of non-linear amplifiers exceeds said first plurality of input signals and said output combining means produces a third plurality of waste energy signals being the difference between said second and said first plurality.

22. The amplifying apparatus of claim 21, wherein said waste energy signals are dissipated in dissipating means to avoid corrupting said desired output signals with intermodulation signals.
23. A method of reducing waste energy in a system for communicating using a first station with a first plurality of second stations using a phased array antenna, comprising the steps of:

   generating the first plurality of signals for transmission to said second stations using radiowave modulation;

   combining said first plurality of signals to produce a second plurality of signals, said combined signals being complex-weighted sums of said first plurality of signals, wherein said second plurality corresponds to a number of antenna arrays disposed along a first dimension of said phased array;

   generating a third plurality of signals from said second plurality of signals corresponding to different groups of elements disposed along a second dimension of said phased array;

   amplifying said third plurality of signals to produce wanted and unwanted signals; and

   radiating said wanted signals in desired directions and said unwanted signals in other directions.

24. The method of claim 23, wherein said first station is an orbiting spacecraft.

25. The method of claim 23, wherein said antenna is a directional antenna.

26. The method of claim 24, wherein said antenna is a directional antenna with at least one beam pointing away from the earth.

27. The method of claim 24, wherein said radio wave modulation comprises speech coding, error-correction coding, error-detection coding, and time division multiplex or digital modulation.
28. A system for communicating using a first station with a first plurality of second stations using a phased array antenna comprising:
   signal generation means for generating said first plurality of signals for transmission to respective second stations using radio-wave modulation;
   combining means for producing a second plurality of combined signals being complex-weighted sums of said first plurality of signals, said second plurality corresponding to a number of antenna array elements disposed along a first dimension of said phased array;
   drive signal generation means for producing from each of said second plurality of signals a third plurality of signals corresponding to different groups of elements disposed along a second dimension of said phased array;
   amplifying apparatus for amplifying said third plurality of signals using respective transmit power amplifiers adapted efficiently to transmit constant amplitude signals; and
   antenna means connected to said amplifying apparatus such that wanted signals are radiated in desired directions and unwanted signals are dissipated in other directions.

29. The method of claim 28, wherein said first station is an orbiting spacecraft.

30. The method of claim 28, wherein said antenna is a directional antenna.

31. The method of claim 28, wherein said antenna is a directional antenna with at least one beam pointing away from the earth.
32. The method of claim 28, wherein said radio wave modulation comprises speech coding, error-correction coding, error-detection coding, and time division multiplex or digital modulation.

33. A system for communicating using a first station with a first plurality of second stations using a phased array antenna comprising:
   signal generation means for generating said first plurality of signals for transmission to respective second stations using radio-wave modulation;

   signal processing means for processing said first plurality of signals to produce a second plurality of constant amplitude drive signals;

   amplifying apparatus for amplifying said second plurality of drive signals using transmit power amplifiers adapted efficiently to transmit constant amplitude signals; and

   antenna means connected to said amplifying apparatus for radiating said power amplified signals such that wanted signals are radiated in desired directions and unwanted signals are dissipated in other directions.

34. A system according to claim 33, wherein said first station is a cellular radiotelephone base station connected to a switching center.

35. A system according to claim 33, wherein said second stations are mobile or portable wireless telephones.

36. A system according to claim 33, wherein said radio-wave modulation comprises speech coding, error-correction coding, error-detection coding, and time-division multiplex or digital modulation.
37. A satellite communications system for communicating from at least one ground station via at least one orbiting satellite to a plurality of mobile stations, comprising:

signal generation means for producing a plurality of constant amplitude signals in dependence on signals desired to be communicated to said mobile stations;

power amplifier means adapted to amplify said constant amplitude signals to produce desired and undesired signals; and

antenna means coupled to said power amplifier means such that said desired signals are radiated in the direction of said mobile stations and the undesired signals produced by said signal generation and power amplifier means are radiated in other directions.

38. An efficient transmitter comprising:

a direct current power source;

an amplifier for amplifying a drive signal so as to produce a desired signal and a waste energy signal;

an antenna for transmitting said desired signal;

a plurality of rectifier elements; and

means for combining said rectifier elements so as to transfer energy from said waste energy signal alternating current to the direct power source.

39. An efficient transmitter according to claim 38, wherein said combining means are directional couplers.

40. An efficient transmitter according to claim 38, wherein said combining means are transmission line transformers.
41. An efficient transmitter according to claim 38, wherein said combining means are inductors and capacitors.

42. A method for increasing the battery life of a battery in a handheld radio transmitter/receiver, comprising the steps of:
rectifying waste radio frequency energy not radiated from an antenna in a rectifier to produce a direct current; and
directing said current to said battery.

43. A method for increasing battery life of a battery in a handheld radio transmitter/receiver according to claim 42, further comprising the step of:
diverting energy reflected from said antenna to said rectifier.

44. A device for increasing the battery life of a battery in a handheld radio transmitter/receiver, comprising:
amplifier means for amplifying a transmit signal and sending said transmit signal to an antenna;
a circulation means for diverting energy reflected from said antenna; and
rectifying means for rectifying said energy diverted from said circulator to produce a direct current which is supplied to said battery.

45. A device according to claim 44, wherein said amplifier means includes two transmit power amplifier stages and a power combiner.

46. A device according to claim 45, wherein said power combiner is a directional coupler.
47. A device of claim 45, wherein said power combiner is a hybrid junction.

48. A device according to claim 45, wherein said antenna is connected to one port of said power combiner and said rectifier is connected to another port of said power combiner.

49. A device for increasing the energy efficiency of an amplifier using feedforward linearization, comprising:
   a direct current power source to power said amplifier;
   a first non-linear amplifier for producing a main output signal;
   a second amplifier for amplifying an error signal;
   combining means for combining said error signal with said main signal to produce a corrected sum signal and a waste energy signal; and
   rectifier means for converting said waste energy signal to a direct current that is supplied back to said direct current power source to reduce net power consumption.

50. An efficient transmitter for varying amplitude signals, comprising:
   a direct current power source;
   first and second power amplifiers adapted to amplify constant amplitude signals powered by said direct current source;
   combining means for combining the outputs of said first and second amplifiers to produce a desired varying amplitude signal and a waste energy signal; and
   rectifier means for converting said waste energy signal into a direct current that is coupled back to said direct current power source to reduce net power consumption.
51. An efficient transmitter for transmitting a plurality of signals, comprising:

- a first current power source;
- a plurality of power amplifiers each adapted to amplify one of 5 said signals;
- combining means for combining the outputs of said power amplifiers to produce a desired sum signal and a second plurality of waste energy signals; and
- at least one rectified circuit for converting at least one of said 10 waste energy signals into direct current which is fed back to said direct current source so as to reduce net power consumption.
FIG. 15

ANTENNA

3 dB COUPLER

RECTIFIER

DIRECT CURRENT SOURCE

DRIVE 1

DRIVE 2

152

154

154

150

158
FIG. 19

TRANSMISSION LINE - Z₀

SIGNAL SOURCE
INPUT

DC OUTPUT

204

202

200

206

208

210

212

214

\( \frac{\lambda}{4} Z₁ \)

\( \frac{\lambda}{4} Z₂ \)

\( \frac{\lambda}{4} Z₃ \)

\( \frac{\lambda}{4} Z₀ \)
**INTERNATIONAL SEARCH REPORT**

**A. CLASSIFICATION OF SUBJECT MATTER**

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<td>H03F 3/68, 3/38, 1/00; H04B 7/185, 7/00, 1/04, 1/40</td>
<td>330/124R, 10, 84, 151; 455/12.1, 49.1, 127, 89,</td>
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According to International Patent Classification (IPC) or to both national classification and IPC.

**B. FIELDS SEARCHED**

**Minimum documentation searched (classification system followed by classification symbols)**


**Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched**

NONE

**Electronic data base consulted during the international search (name of data base and, where practicable, search terms used)**

NONE

**C. DOCUMENTS CONSIDERED TO BE RELEVANT**

<table>
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<th>Citation of document, with indication, where appropriate, of the relevant passages</th>
<th>Relevant to claim No.</th>
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<tr>
<td>X</td>
<td>US, A, 3,917,998 (WELTI) 04 November 1975 See figures 2-3.</td>
<td>20</td>
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<tr>
<td>Y</td>
<td>US, A, 5,264,807 (OKUBO et al) 23 November 1993 See figure 5, blocks 21, 22-23, 30, column 9, lines 27-68, column 10, lines 1-7.</td>
<td>15, 14-19, 21-22</td>
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</table>

Further documents are listed in the continuation of Box C. See patent family annex.

**Date of the actual completion of the international search**

31 MARCH 1995

**Date of mailing of the international search report**

16 MAY 1995

**Name and mailing address of the ISA/US**

Commissioner of Patents and Trademarks
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NGUYEN VO

**Telephone No.** (703) 308-6728

Form PCT/ISA/210 (second sheet)(July 1992)*
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<td>Y</td>
<td>US, A, 4,901,085 (SPRING et al) 13 February 1990 See figure 1, column 2, lines 33-68, column 3.</td>
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<td>A</td>
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<td>23-32</td>
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<tr>
<td>Y</td>
<td>US, A, 3,649,927 (SEIDEL) 14 March 1972 See figure 1, column 2.</td>
<td>38-51</td>
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<tr>
<td>Y</td>
<td>US, A, 4,319,359 (WOLF) 09 March 1982 See column 2, lines 48-55, column 5, lines 37-40.</td>
<td>38-51</td>
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<tr>
<td>A</td>
<td>US, A, 4,068,186 (SATO et al) 10 January 1978 See figures 3A-3B, columns 4-5.</td>
<td>1-22</td>
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<tr>
<td>A</td>
<td>US, A, 4,618,831 (EGAMI et al) 21 October 1986 See figure 3, column 4, lines 35-68, column 5, lines 1-10.</td>
<td>1-22</td>
</tr>
<tr>
<td>A</td>
<td>US, A, 5,012,254 (THOMPSON) 30 April 1991 See figure 2, column 5, lines 42-68, column 6, lines 1-26.</td>
<td>23-37</td>
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<tr>
<td>A</td>
<td>US, A, 5,093,668 (SREENIVAS) 03 March 1992 See figure 3, column 5, lines 42-68, column 6, lines 1-56.</td>
<td>23-37</td>
</tr>
<tr>
<td>A</td>
<td>US, A, 4,899,162 (BAYETTO et al) 06 February 1990 See figure 4, column 4, lines 25-47.</td>
<td>23-37</td>
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<tr>
<td>A</td>
<td>US, A, 5,119,042 (CRAMPTON et al) 02 June 1992 See figure 3, column 6, lines 53-68, column 7.</td>
<td>23-37</td>
</tr>
<tr>
<td>A</td>
<td>US, A, 4,595,882 (SILAGI et al) 17 June 1986 See figure 2, columns 5-6.</td>
<td>38-51</td>
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INTERNATIONAL SEARCH REPORT

Box I Observations where certain claims were found unsearchable (Continuation of item 1 of first sheet)

This international report has not been established in respect of certain claims under Article 17(2)(a) for the following reasons:

1. ☐ Claims Nos.: because they relate to subject matter not required to be searched by this Authority, namely:

2. ☐ Claims Nos.: because they relate to parts of the international application that do not comply with the prescribed requirements to such an extent that no meaningful international search can be carried out, specifically:

3. ☐ Claims Nos.: because they are dependent claims and are not drafted in accordance with the second and third sentences of Rule 6.4(g).

Box II Observations where unity of invention is lacking (Continuation of item 2 of first sheet)

This International Searching Authority found multiple inventions in this international application, as follows:

   Telephone Practice
   Please See Extra Sheet.

1. ☑ As all required additional search fees were timely paid by the applicant, this international search report covers all searchable claims.

2. ☐ As all searchable claims could be searched without effort justifying an additional fee, this Authority did not invite payment of any additional fee.

3. ☐ As only some of the required additional search fees were timely paid by the applicant, this international search report covers only those claims for which fees were paid, specifically claims Nos.:

4. ☐ No required additional search fees were timely paid by the applicant. Consequently, this international search report is restricted to the invention first mentioned in the claims; it is covered by claims Nos.:

Remark on Protest ☐ The additional search fees were accompanied by the applicant’s protest.

☐ No protest accompanied the payment of additional search fees.

Form PCT/ISA/210 (continuation of first sheet(1))(July 1992)
B. FIELDS SEARCHED
Minimum documentation searched
Classification System: U.S.
330/124R, 10, 84, 151, 295, 149, 136, 297, 202; 455/12.1, 49.1, 127, 89, 343, 11.1, 13.3, 13.4, 129, 54.1, 33.1;
379/59; 343/853, DIG2, 342/372, 373.

BOX II. OBSERVATIONS WHERE UNITY OF INVENTION WAS LACKING
This ISA found multiple inventions as follows:


2. Grouping of inventions:
   - Group I, claims 1-3, drawn to a plural amplifier channel.
   - Group II, claims 4-19, drawn to a modulator-demodulator-type amplifier.
   - Group III, claims 20-22, drawn to a plural amplifier channel with signal feedback.
   - Group IV, claims 23-32, and 37, drawn to a satellite communications system.
   - Group V, claims 33-36, drawn to a wireless communications system.
   - Group VI, claims 38-41, and 50-51, drawn to a radio transmitter for controlling waste energy.
   - Group VII, claims 42-48, drawn to a handheld radio transmitter/receiver for controlling waste energy.
   - Group VIII, claim 49, drawn to an amplifier with forward feeding.

3. The inventions listed as Group I to Group VIII do not meet the requirements for Unity of invention because they are not connected in design, have different modes of operation, different functions or different effects. One invention does not require another to operate properly. Therefore, the inventions describe different functions or different effects which are directed to different special technical features in relation to each group of inventions.