July 15, 1969 L. R. PEASLEE Re. 26,630

VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

Original Filed Aug. 7, 1961 12 Sheets-Sheet 1

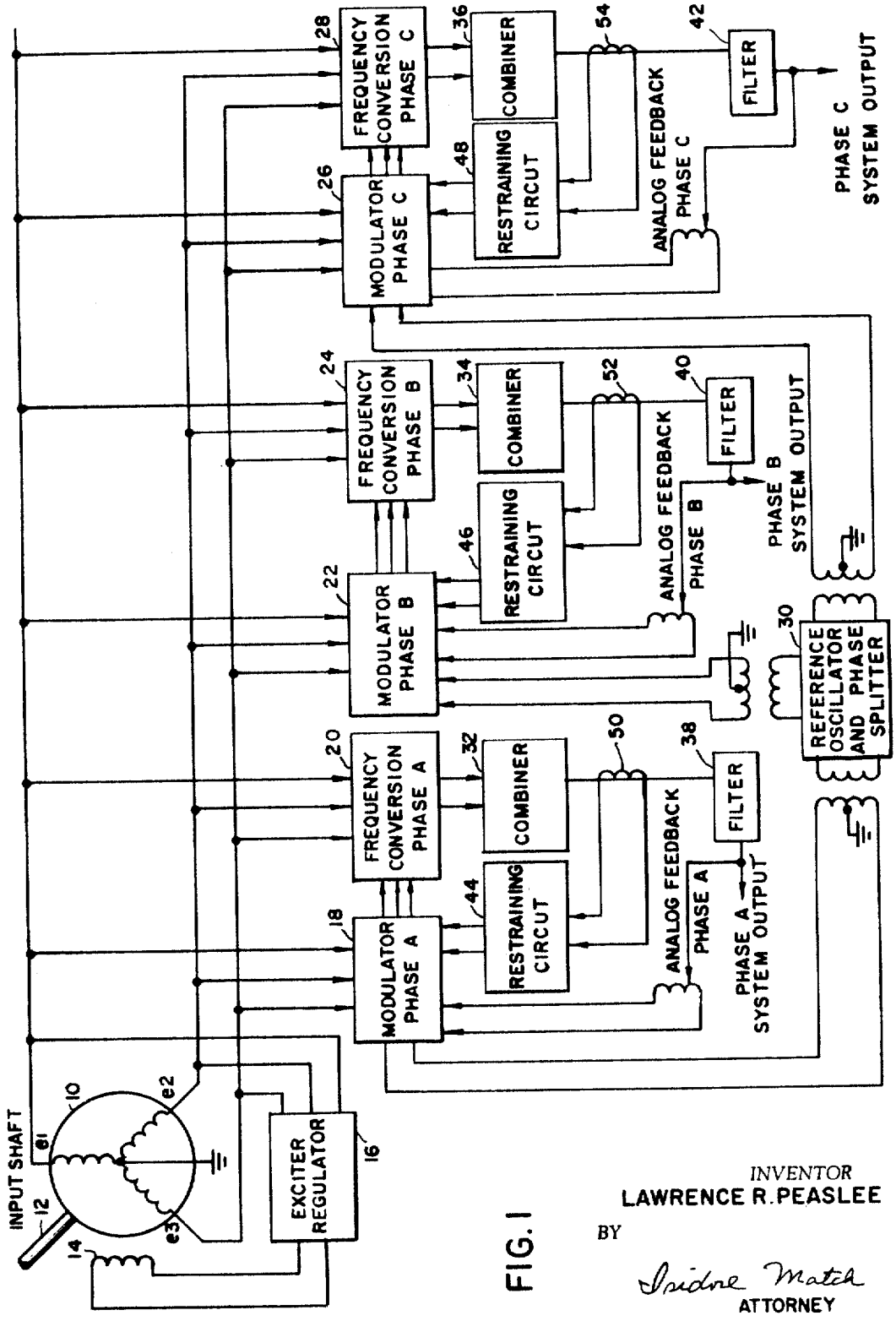


FIG. 1

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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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FIG. 2

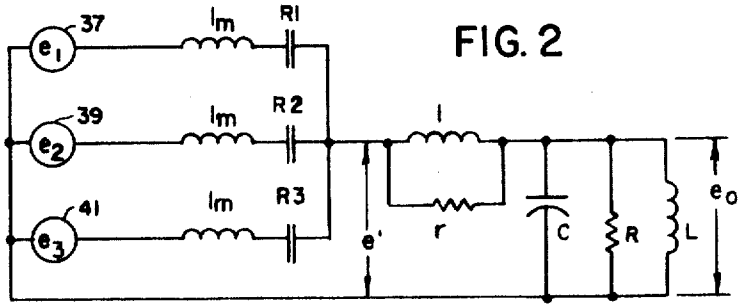


FIG. 7

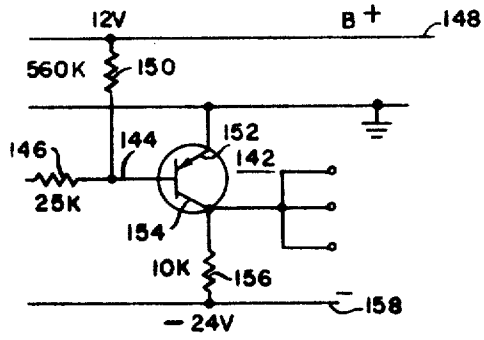


FIG. 8

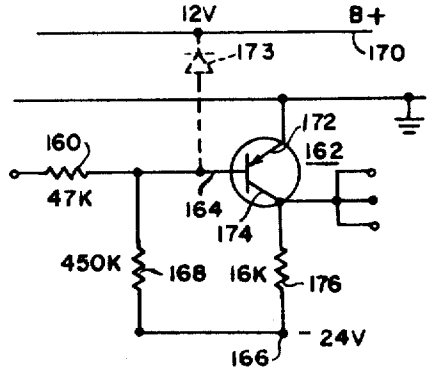
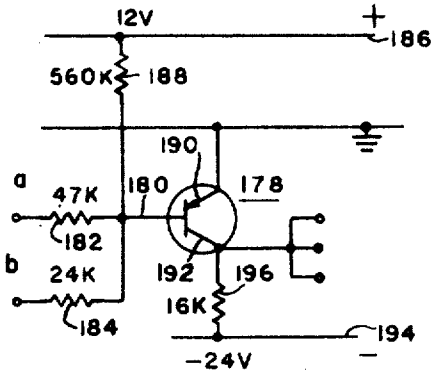


FIG. 9



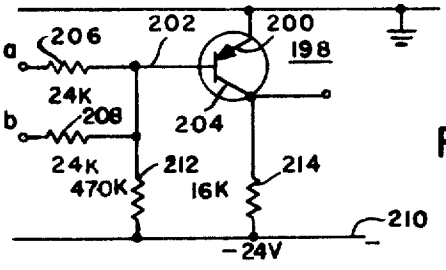
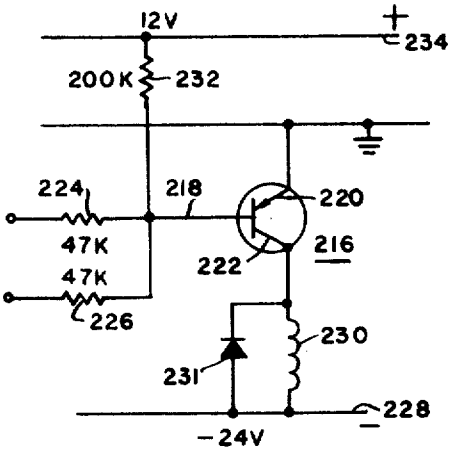


FIG. 10

FIG. 12



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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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FIG. 3

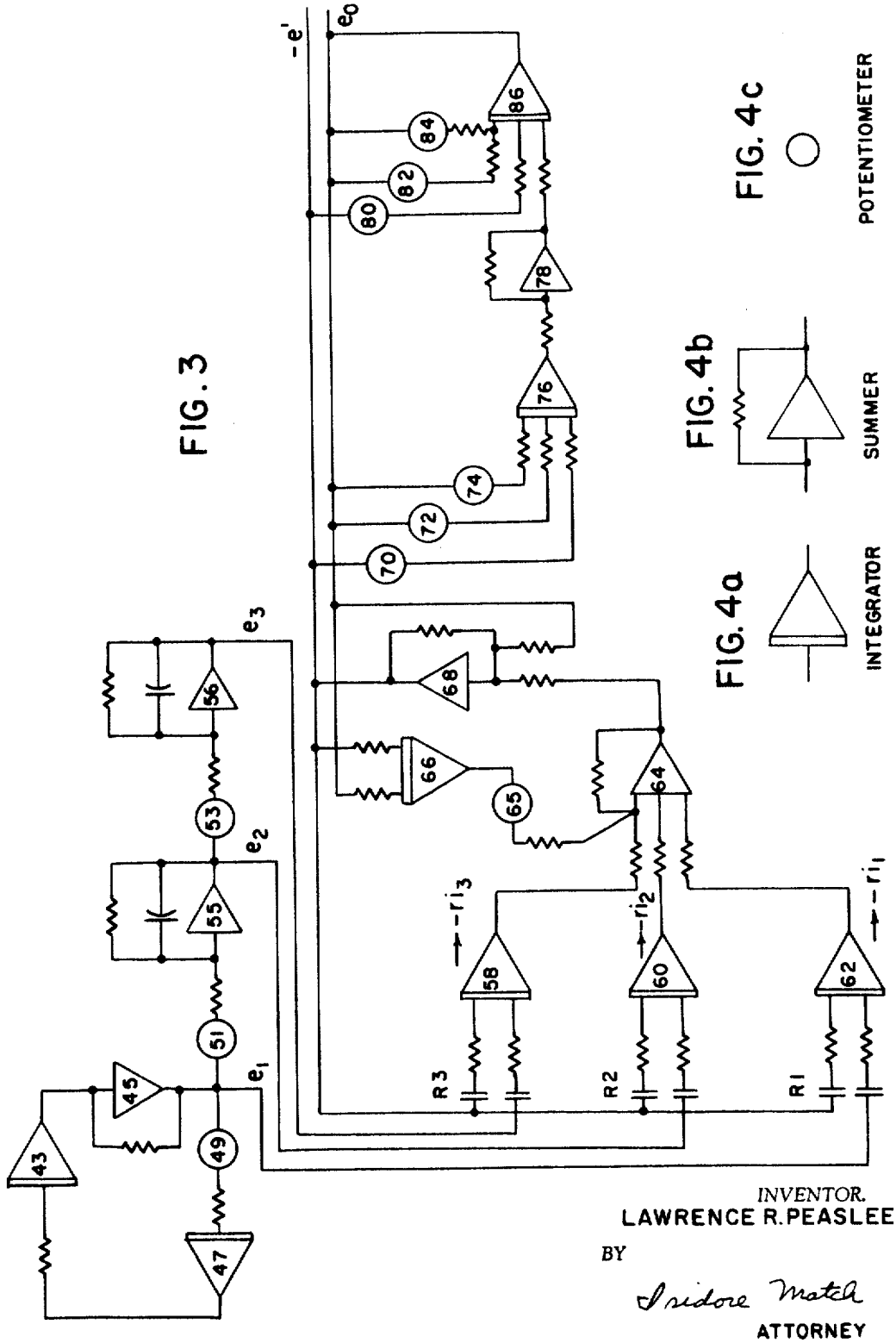


FIG. 4c

FIG. 4b

FIG. 4a

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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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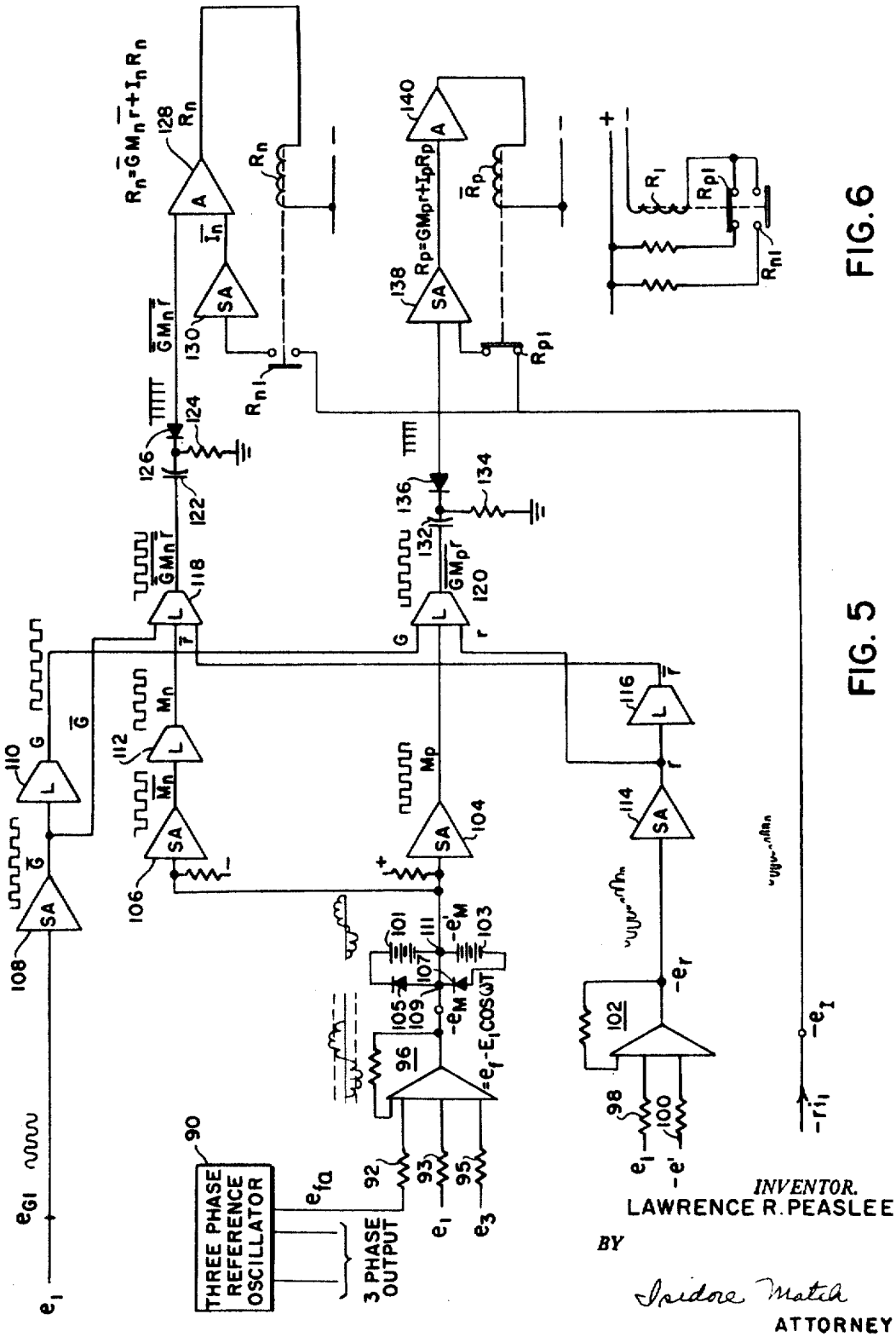


FIG. 6

FIG. 5

VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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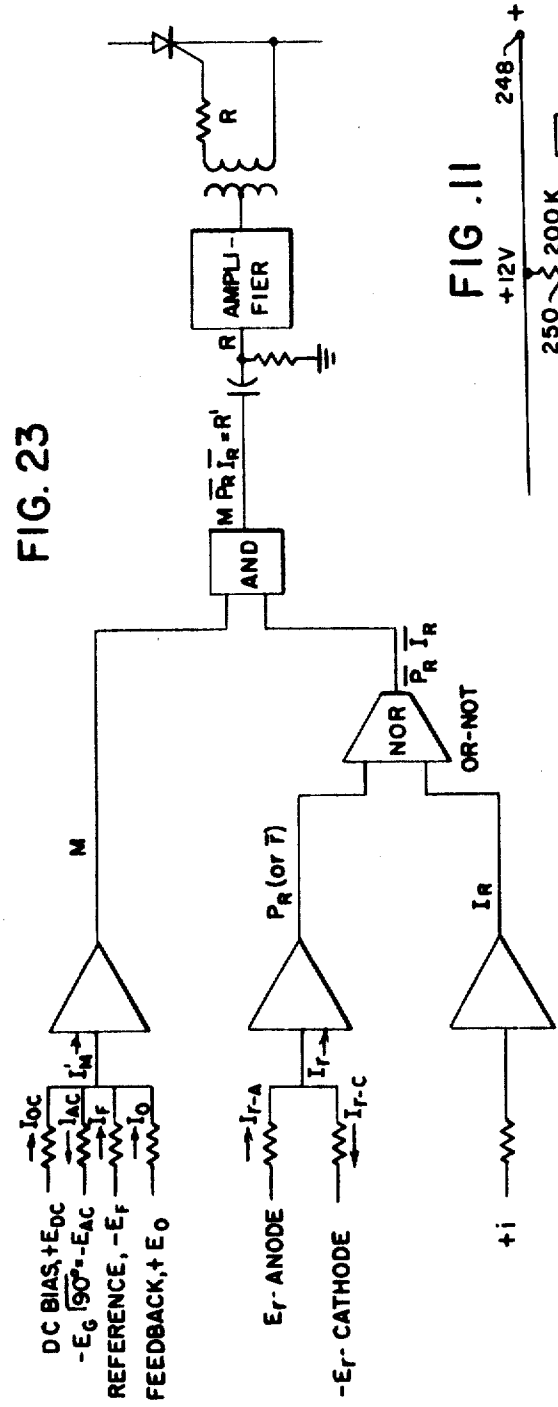


FIG. 23

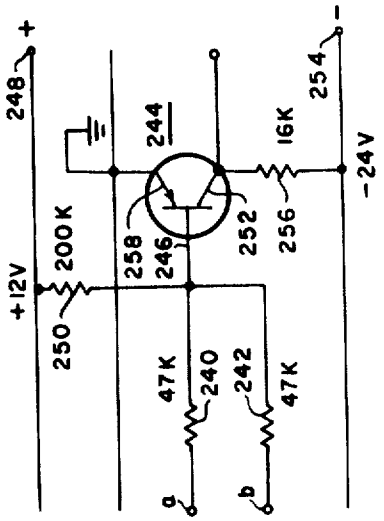


FIG. 11

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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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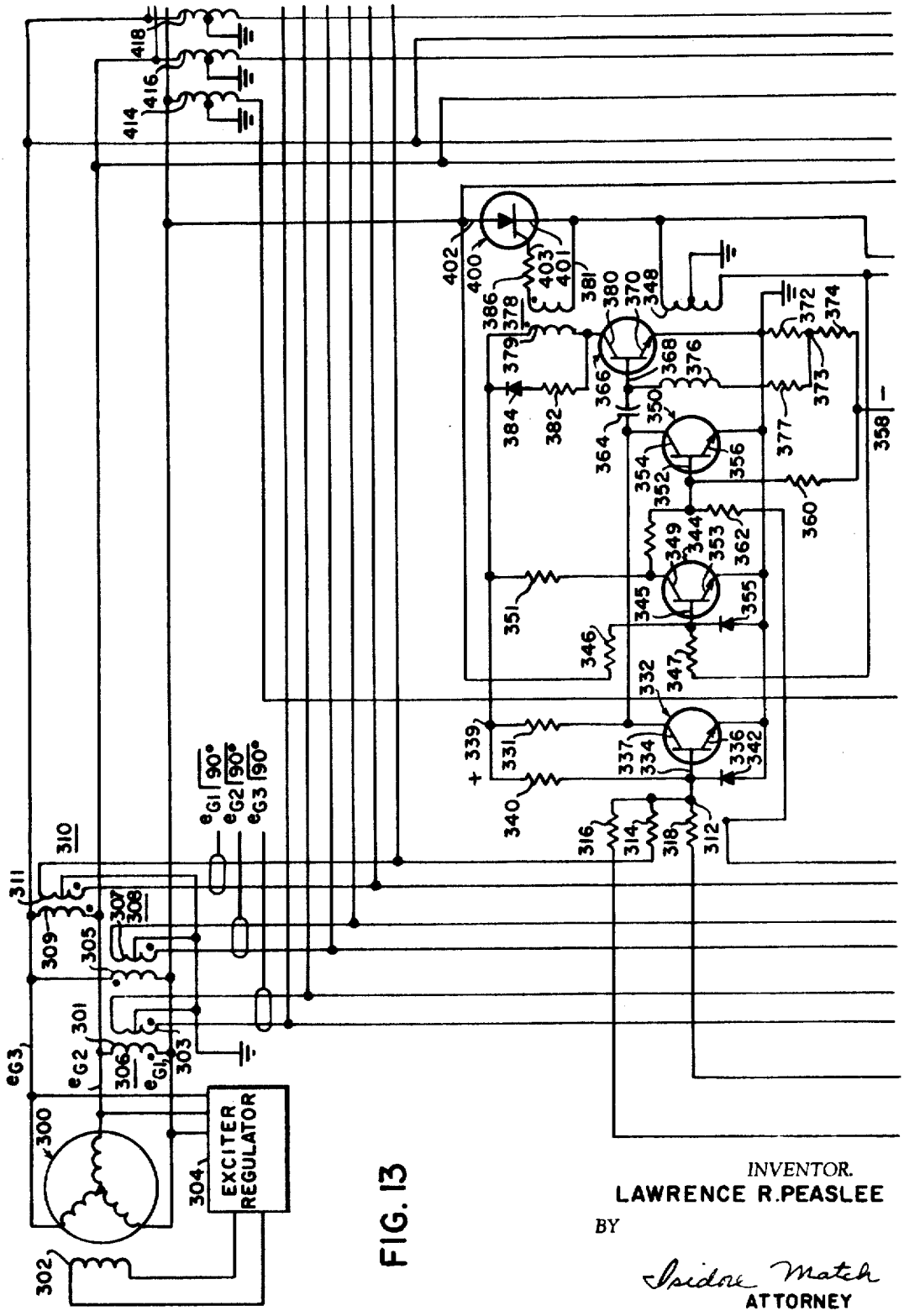


FIG. 13

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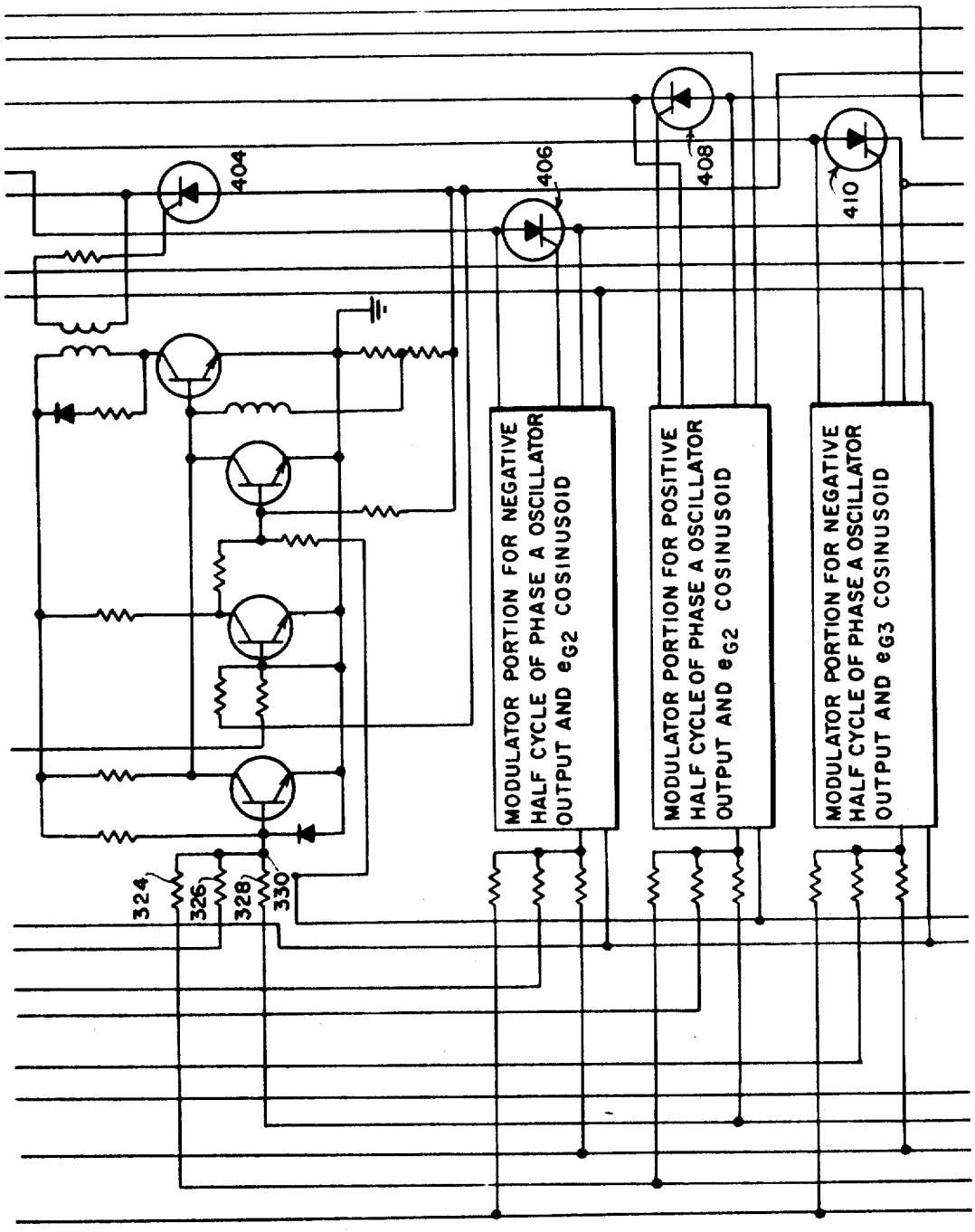


FIG. 14

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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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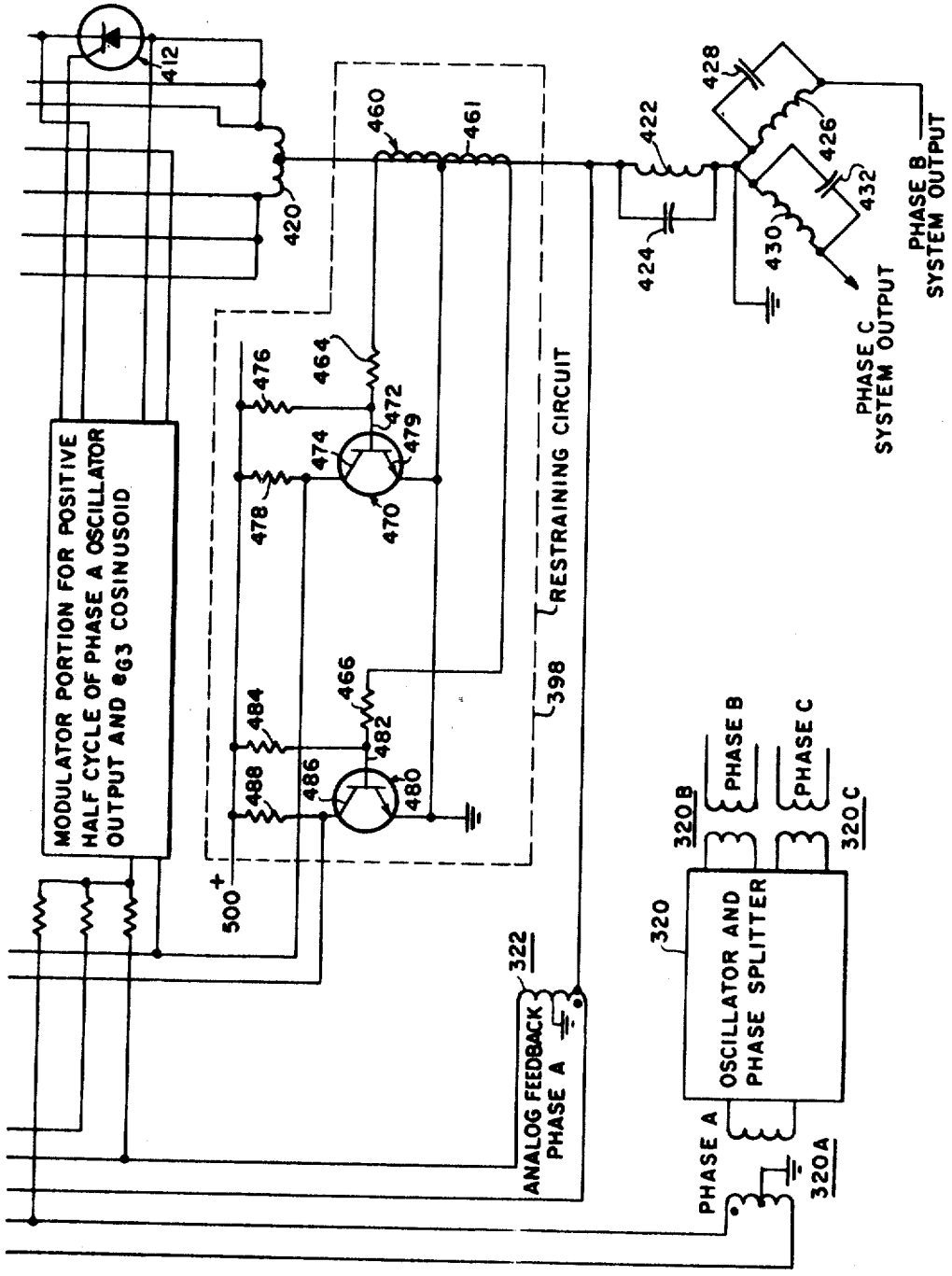


FIG. 15

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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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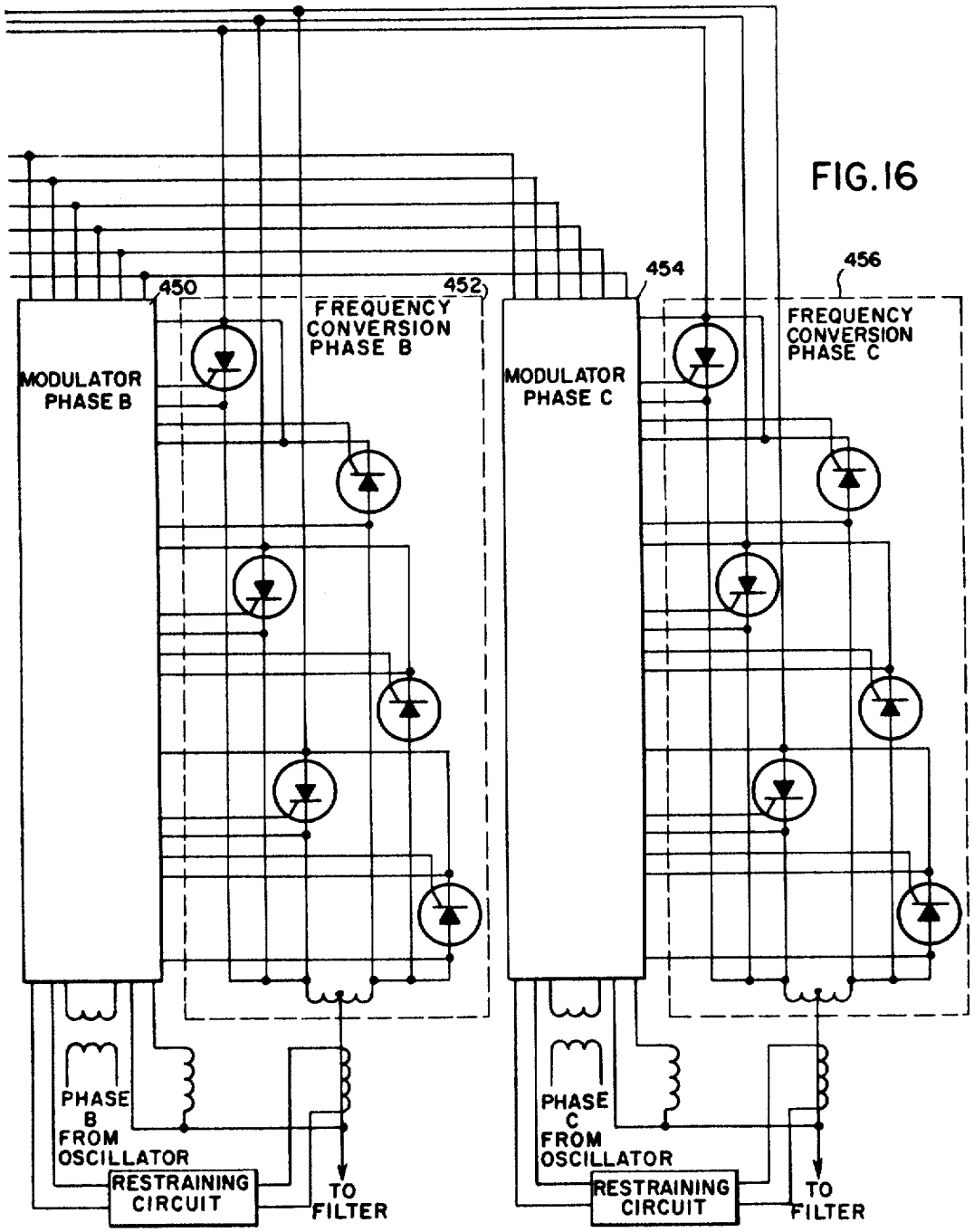


FIG. 16

FIG. 17

FIG. 13	FIG. 16 17
FIG. 14	
FIG. 15	

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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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FIG. 18

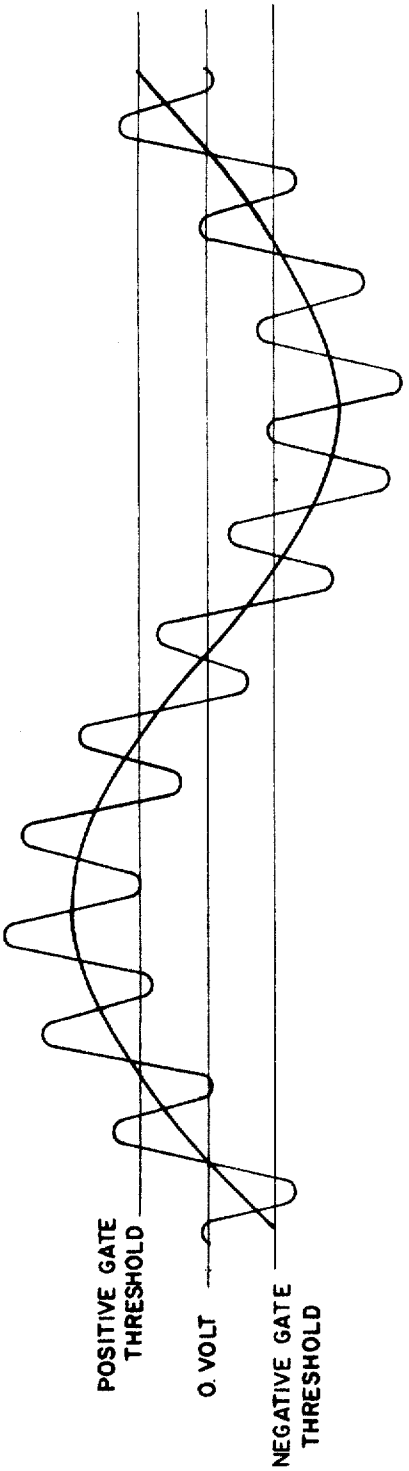


FIG. 21

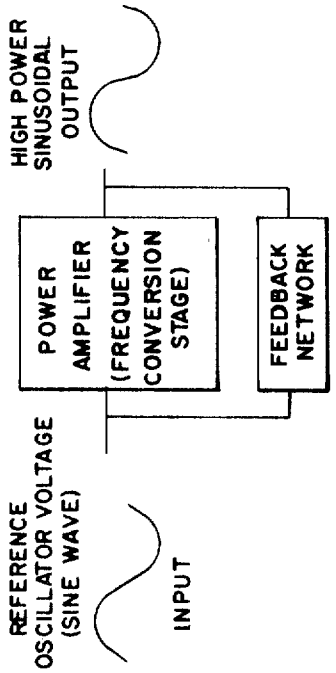
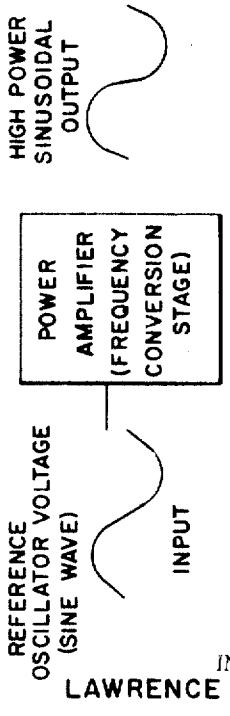


FIG. 20



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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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FIG. 19a

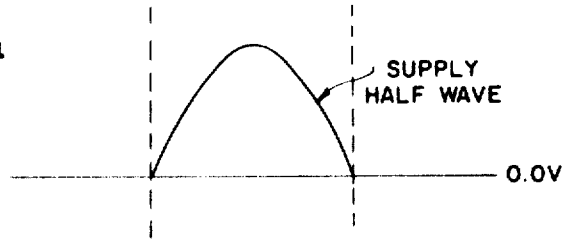


FIG. 19b

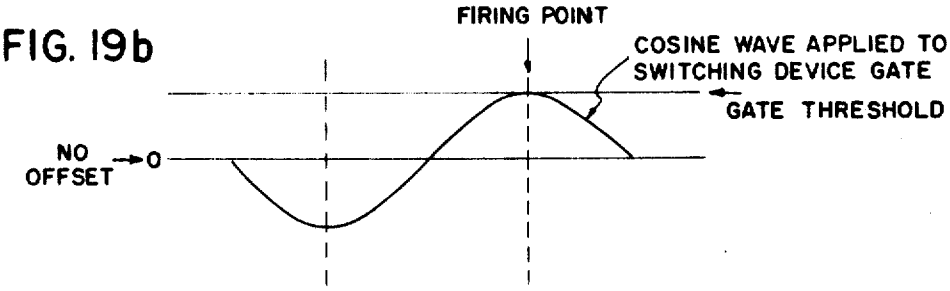


FIG. 19c

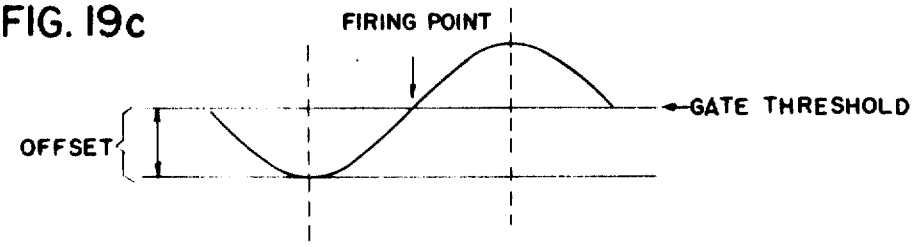
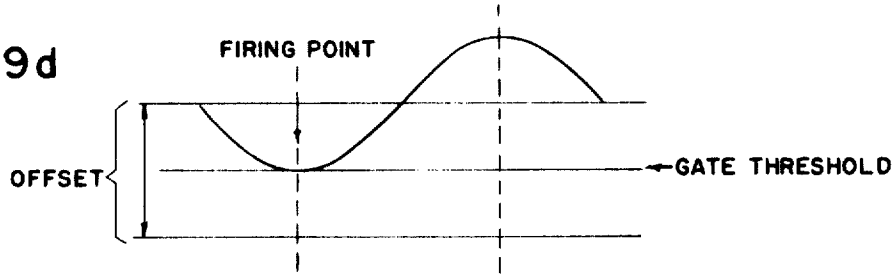


FIG. 19d



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VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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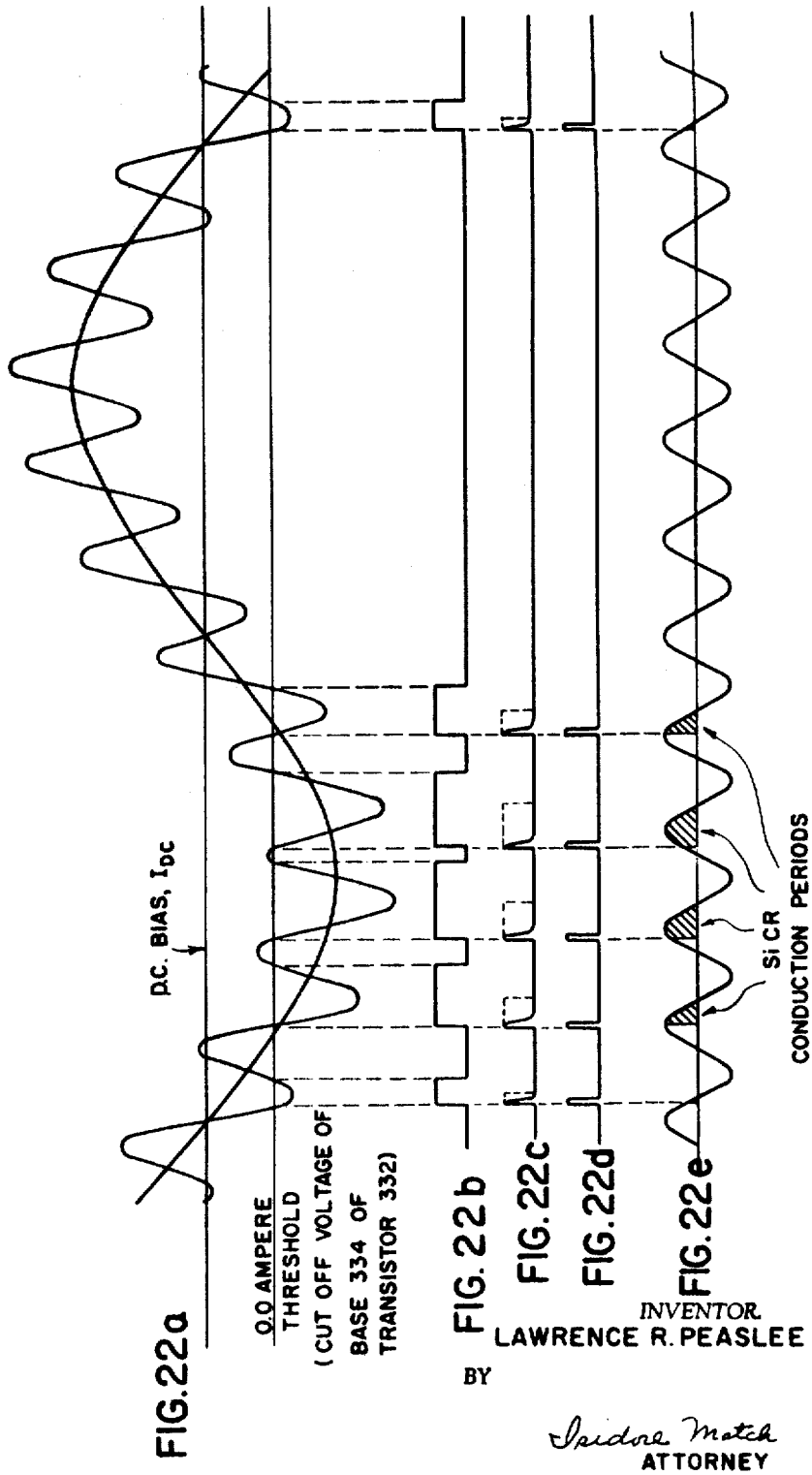


FIG. 22a FIG. 22b FIG. 22c FIG. 22d FIG. 22e

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United States Patent Office

Re. 26,630
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26,630
VARIABLE SPEED CONSTANT FREQUENCY SYSTEM

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Original No. 3,152,297, dated Oct. 6, 1964, Ser. No. 129,646, Aug. 7, 1961. Application for reissue May 25, 1966, Ser. No. 559,031

Int. Cl. H02m *1/08*

U.S. Cl. 321—69 13 Claims

Matter enclosed in heavy brackets [ ] appears in the original patent but forms no part of this reissue specification; matter printed in italics indicates the additions made by reissue.

This invention relates to frequency converter systems. [More particularly, it relates to a system for providing an output having a range of determinate frequencies from a variable speed source.] *In copending application Ser. No. 536,149 filed Mar. 21, 1966 by D. L. Plette (which is a continuation of application Ser. No. 122,278, filed July 6, 1961, and which is assigned to the same assignee as this present application) there is disclosed a frequency conversion system for providing a range of determinate frequencies from a variable speed source.*

Copending application Ser. No. 562,032, filed June 2, 1966 by L. R. Peaslee and S. C. Caldwell (which is a reissue application of U.S. Patent 3,148,324 and which is assigned to the same assignee as this present application) and the present application disclose and claim improvements on the invention of Plette. The claims in the Peaslee-Caldwell application are directed to a frequency conversion system in which the modulation function is improved by sinusoidal to cosinusoidal signal conversion and also by the addition of means to insure that gating signals are applied to the switching devices only when these devices are in a conductive condition. The claims in the present application are directed to a frequency conversion system having analog feedback to improve the output waveshape.

In many situations such as aircraft systems or other arrangements wherein an engine whose speed varies over a wide range is utilized to power an electric generator, it has been desirable to obtain a constant frequency output having a chosen range of determinate frequencies from the variable speed source provided by such engine. Heretofore, the most widely used device for this purpose has been a hydraulic constant speed drive which is essentially a hydraulic generator-motor system that utilizes either a variable displacement generator or a motor in continuously variable ratio over a requisite input speed range.

Such transmissions which are in general use today are quite complex and require extreme precision of moving parts together with associated piping and cooling systems. In addition, the lives of such systems are relatively short and considerable maintenance thereof is required. Also, overhead costs of such systems are high and development costs for new ratings and speed ranges plus the production costs thereof are quite expensive. The speed limitations of these systems serve to inhibit the development of lighter weight systems.

It is, accordingly, an important object of this invention to provide an all-electrical system for converting the indeterminate variable shaft speed provided by an engine or other energy source to an electrical output having a chosen range of determinate frequencies.

It is a further object to provide a system in accordance with the preceding object which is relatively light in weight and has a relatively large power handling capacity.

It is another object to provide a system in accordance with the preceding objects wherein considerable flexibility and selection of input speed range and output frequency is enabled and wherein the efficiency of the system is high.

Generally speaking and in accordance with the invention, there are provided in combination, first means to produce a plurality of like outputs equally displaced in phase and having an indeterminate variable frequency, a source of reference voltage having a given range of determinable frequencies, the highest frequency of the range generally being less than the lowest frequency of the outputs and second means in circuit with the reference voltage source and the first means for mixing the outputs and the reference voltage. There are also included third means in circuit with the first means to produce first signal conditions in response to half cycles of one polarity of the outputs and second signal conditions in response to half cycles of the opposite polarity of the outputs and fourth means in circuit with the second and third means for producing first and second signals during such signal conditions in response to the application of the resultant of the mixing of the outputs and the reference voltage. Means are further included to combine the signals to produce an output having the frequency of the reference voltage.

The features of this invention which are believed to be new are set forth with particularity in the appended claims. The invention itself, however, may best be understood by reference to the following description when taken in conjunction with the accompanying drawings which show embodiments of a frequency converter according to the invention.

In the drawings,

FIG. 1 is a block diagram of a system in accordance with the invention;

FIG. 2 is a diagram conveniently utilized for explaining the inventive concept of the system;

FIG. 3 is a block depiction of an arrangement for providing output signals in accordance with a simulated embodiment of the system;

FIGS 4a–4c are depictions of the circuit symbols utilized in FIG. 3;

FIG. 5 is a diagram of a portion of a modulator which is utilized in the simulated embodiment;

FIG. 6 is a diagram useful in explaining the operation of the system of FIG. 5;

FIGS. 7–12 are schematic diagrams of circuits utilized in the modulator of FIG. 5; and

FIGS. 13–16 taken together as in FIG. 17 is a diagram of another embodiment of the system;

FIG. 18 is a depiction of a waveform useful in explaining the operation of the invention;

FIGS. 19a–19d comprise a timing diagram of waveforms useful in explaining the operation of the invention;

FIGS. 20 and 21 illustrate the feedback feature of the invention;

FIGS. 22a–22e comprise a timing diagram of wave forms which occur in the operation of the embodiment depicted in FIGS. 13–17; and

FIG. 23 is a logical diagram depicting the operation of the embodiment shown in FIGS. 13–17.

Referring now to FIG. 1 wherein there is shown an embodiment of a system in accordance with the invention, a generator **10** in response to the application thereto of the variable speed power from shaft **12** produces a three phase output, viz, phase e_1, e_2 and e_3 having a frequency in accordance with the speed of shaft **12**. The field winding **14** of generator **10** is excited by an exciter **16** which may suitably be of the static type, there being fed back to a voltage regulator contained in exciter **16**, the phase e_1, e_2 and e_3 outputs of the generator **10** to provide thereby voltage regulation of the outputs of generator **10**.

For providing three outputs from the system which are

equally displaced in phase, viz., phases A, B and C, a modulator and a frequency conversion stage are provided for producing each output. Thus, for phase A, there are provided a modulator **18** and a frequency conversion stage **20**. For phase B, there are provided a modulator **22** and a frequency conversion stage **24**, and for phase C, there are provided a modulator **26** and a frequency conversion stage **28**. An oscillator and phase splitter **30** having a three phase output of a given range of determinable frequencies provides a reference frequency voltage for modulators **18**, **22** and **26**.

In the frequency conversion stages **20**, **24** and **28**, there are included power switching devices which are rendered conductive in response to switching signals respectively applied thereto to perform the frequency conversions in the system. The outputs of the frequency conversion stages **20**, **24** and **28** are combined in combiners **32**, **34** and **36**, respectively. Since the unfiltered outputs of the combiners contain components having undesired frequencies, the output filters **38**, **40** and **42** substantially remove such undesired components.

In the modulators, one of the respective phase outputs of oscillator **30** is mixed with the three phase outputs of generator **10** to provide the proper switching signals for the power switching devices in the frequency conversion stages respectively. The exciter regulator **16** functions to control the excitation in generator **10** so that the proper voltages are applied to the frequency converters.

Oscillator stage **30** contains an oscillator, the frequency of the output of which determines the frequency of the output of the system. The three balanced phase outputs from oscillator stage **30** are derived by means of a phase splitter or like device, which determines the system phase displacement and phase sequence. The frequency of generator **10** is suitably chosen to be about 4 to 20 times the oscillator frequency.

Analog feedbacks of the respective system phase outputs to the corresponding modulators serve to reduce distortion of the output of the system and also to provide a degree of voltage regulation.

In the frequency conversion stages, a plurality of first switching devices is controlled by the positive half cycles of the outputs of generator **10** and another such plurality of second switching devices is controlled by the negative half cycles of the outputs of generator **10**. The restraining circuits **44**, **46** and **48** serve to insure that no commutation occurs between the respective first and second pluralities of switching devices in an associated frequency conversion stage unless the current in the output of the associated combiner is passing through or already has passed through the zero crossover point. The currents in the outputs of combiners **32**, **34** and **36**, respectively, are sensed by current transformers **50**, **52** and **54**, the current in transformers **50**, **52** and **54** being fed to restraining circuits **44**, **46** and **48** respectively.

In FIG. 2, there is shown a circuit which depicts the circuit relationships in one phase of the system of the invention. In this circuit, the generators **37**, **39**, **41** produce the three outputs 120° displaced in phase with respect to each other, each output, viz, voltages e_1, e_2 and e_3 having the same varying frequency. The series inductance l_m represents the total commutating inductance of the system. The normally open relay contacts R_1, R_2 and R_3 which represent the nonconductive conditions of the switching devices in a frequency conversion stage of FIG. 1, when they assume the closed position, switch the output of the system from one generator phase to another as effected by gating signals applied to the switching devices (not shown) respectively associated with contacts R_1, R_2 and R_3.

In the operation of the circuit of FIG. 2, the switching devices associated with contacts R_1, R_2 and R_3, respectively, are energized in accordance with the output of a modulator (FIG. 5) wherein the three balanced generator voltages e_1, e_2, e_3 are mixed with a reference voltage having a determinate frequency. Preferably the frequency of the reference voltage is such that the range of frequencies of the generator voltages is about from four to twenty times [as great thereof] *greater*. Of course, three reference voltages are provided where there are three frequency converter stages and are equally displaced in phase with respect to each other as are the generator voltages, the mixing occurring in each phase in the modulator between the three phase generator voltages and one of the reference voltage phases.

The output passed through alternately closed contacts R_1, R_2 and R_3 is filtered through filter inductance l and capacitance C and developed across load inductance L and resistance R to provide the output voltage e_0 for a system phase output.

In the circuit of FIG. 2, in the relationships obtaining therein, as shown hereinbelow, classical notation rather than operational notation is utilized to more directly preserve identification between measured quantities and the physical components of the actual system. The relationships are:

$$e_1=e_1 \sin 2\pi f_g t;\ e_2=a^2e_1;\ e_3=ae_1;\ a=e^{j120°}$$

where

f_g=generator frequency

$e_0=e_0 \sin 2\pi f_0 t$ where f_0=output frequency

$l_m \cong l_d$

with no amortisseurs (generator transient inductance)

$$l_m \cong l_d''$$

with amortisseurs (generator sub-transient inductance)

l=filter inductance

L=load inductance

C=filter capacitance

r=equivalent resistance of the core loss in inductance l

R=load resistance

The current equations of the system are:

$$i=\Sigma \frac{1}{l_m}\int (e_i-e')\ dt \qquad (a)$$

$$i=\frac{1}{l}\int (e'-e_0)\ dt+\frac{1}{r}\ (e'-[e^0]\ e_0) \qquad (b)$$

$$i=\frac{1}{L}\int e_0\ dt+C\frac{de_0}{dt}+\frac{1}{R}\ e_0 \qquad (c)$$

where $e_i=e_1$, e_2 or e_3 whichever is connected to the filter input at the time considered.

Equation a represents the current flowing in the generator and may consist of: no currents, current in one phase or current in two phases depending upon the condition of the system at the time considered. Equation b represents the sums of the currents flowing through the inductance and resistance branches, l and r of FIG. 2. Equation c represents the total current flow into the shunt branches C, R and L in FIG. 2.

When Equations a and b are solved simultaneously there results:

$$e'=\Sigma\left[\frac{r}{l_m}\int (e_i-[e^1]\ e')\ dt\right]-\frac{r}{l}\int ([e^1-e^0]\ e'-e_0)\,dt \qquad (d)$$

and when Equations b and c are solved simultaneously, there results:

$$e_0=\int\left[\frac{1}{lC}\int ([e^1]\ e'-e_0)\ dt-\frac{1}{LC}\int e_0\ dt+\frac{1}{rC}\ ([e^1]\ e'-e_0)-\frac{1}{RC}\ e_0\right]dt \qquad (e)$$

In FIG. 3, there is shown a circuit for producing the three balanced generator voltages e_1, e_2 and e_3 and output voltages e_0 and e' as set forth in Equations d and e. In FIGS. 4a, 4b and 4c, there are shown the symbols uti-

lized in depicting the system elements in the circuit of FIG. 3.

In the circuit of FIG. 3, Equation d is represented by integrators **58**, **60**, **62** and **66** and summers **64** and **68**. The outputs of integrators **58**, **60** and **62** are respectively equal to the currents in phases e_1, e_2 and e_3 multiplied by the factor "r" (FIG. 2). The output of integrator **66** is the factor "r" times the current in the inductive branch of the series filter inductor 1 (FIG. 2), and the current in the resistive branch of the series filter is the factor

$$\frac{\text{"1"}}{r}$$

times the difference between e' and e_0. The system output voltage is e_0.

Equation e is represented in FIG. 3 by integrators **76** and **86** and summer **78**. The potentiometers **49**, **51**, **53**, **65**, **70**, **72**, **74**, **80**, **82** and **84** may be utilized in varying the system loading with each potentiometer being a loading element. Integrators **43** and **47**, together with summers **45**, **55** and **56** provide the three phase voltage source, viz, voltages e_1, e_2 and e_3.

In FIG. 5, there is shown a portion of a modulator circuit which may be utilized with the computer circuit of FIG. 3. The circuit of FIG. 5 essentially has two functions, viz, the supplying of the necessary information to fire the simulated switching devices therein (silicon controlled rectifiers being the type of devices that are simulated), according to a predetermined schedule (as modified by an analog feedback signal) and to provide additional logic to the simultated silicon controlled rectifiers whereby they properly perform all the functions of silicon controlled rectifiers.

In this figure, the output of one phase of a polyphase variable frequency oscillator **90**, which can be conveniently designated as voltage e_{fa} is applied through a resistor **92** as one input to a D.C. amplifier **96**. Also, applied through resistors **93** and **95** as inputs to D.C. amplifier **96** are the generator phase outputs e_1 and e_3. Resistor **93** is chosen to have a value which is twice the value of resistors **92** and **95**. Since signals e_1 and e_3 are 120° displaced in phase with respect to each other, the output of amplifier **96** may be conveniently designated as $-e_M=e_{fa}-\cos e_1$. In FIG. 18 there is shown the wave shape of the signal e_M. In this wave shape, if the amplitude of the output of the oscillator wave is taken to have a value of "one," then the amplitude of the generator voltage superimposed thereon is "one-half." The positive gate threshold line in FIG. 18 also has an amplitude of one-half and indicates the voltage level above which a silicon controlled rectifier controlled by a positive half cycle of generator voltage is switched into conductivity. The line in FIG. 18 designated "negative gate threshold" indicates the voltage below which a silicon controlled rectifier controlled by the negative half cycles of generator output is switched into conductivity.

It is to be noted that the generator signal superimposed on the oscillator signal in FIG. 18 is a cosinusoid. This is readily appreciated that from the fact that since e_1 and e_3 are 120° displaced in phase with respect to each other and since the value of resistor **93** is twice that of resistor **95**, the summing in amplifier **96** provides the cosinusoid of the e_1 voltage.

Prior to describing the remainder of the modulator of FIG. 5, it is to be realized that the purpose of this modulator is to construct a firing schedule which will produce the best sine wave power output for a given filter or, conversely, to produce a sine wave of a given quality with the least filtering. In this connection, it is to be noted that the filter itself is not the only part affected. Thus, if the filter series inductance increases in size, the generator must also increase in size to supply the added voltage drop across such inductance.

It has been found that if the generator output is directly superimposed on the reference oscillator wave, in the

event that there are present different power factors in the generator output, the sine waves from the generator superimposed upon the oscillator wave are distorted. Accordingly, it is first desired to vary the firing angle of the switching device as a function of the instantaneous height of the firing curve.

The latter can be accomplished by producing a cosinusoid from the generator voltage and utilizing it, as shown in FIGS. 19a–d. In FIG. 19a there is shown a half cycle of voltage from a generator output. In FIG. 19b, there is shown a cosine wave derived from the wave of FIG. 19a with no offset. In FIG. 19c there is shown the same cosine wave with an offset whereby the gate threshold is at the crossover point of half cycles of the cosinusoid. In FIG. 19d, there is shown a cosinusoid wave with an offset whereby the gate threshold is at the most negative point of the wave. It is seen from FIGS. 19c and 19d that if a cosinusoid having the same frequency as the generator output is varied up and down with an offset, the point at which the switching device is actuated can readily be varied from 0° to 180°. Thus, if the cosinusoid is added to the oscillator wave as shown in FIG. 18, the firing angle can be made to progress smoothly from conduction periods of 0° to full conduction and back to 0° as the curve rises and falls.

To obtain such performance, gate thresholds and magnitudes are set as has been described in connection with FIG. 18. In FIG. 18, the amplitude of the oscillator wave, is taken to be one, the amplitude of the cosinusoid taken to be one-half and the amplitudes of the positive and negative gate thresholds, respectively, are plus and minus one-half. With this arrangement, there is enabled a variation of conduction angle in the switching device as a function of the instantaneous oscillator wave magnitude.

It is also desired to shape the firing curve as a function of load and power factor to produce the best sine wave output from the filter. It is realized that a modulator and a frequency conversion stage (FIG. 1) together provide a power amplifier of considerable power gain as shown in FIG. 20. Parts of the converter are extremely non-linear but the operation desired is that of a high power linear amplifier. To linearize the power amplifier, feedback is utilized such as shown in FIG. 21. With feedback, the power gain is reduced. However, the obtainable power gain with switching devices is very great. Accordingly, the power of the reference voltage may be small proportionately.

The feedback signals obtained from the output voltage (FIG. 21) may be considered as consisting of two parts; a first type feedback comprising the fundamental output frequency and its harmonics and a second type feedback comprising the modulated ripple voltage derived from the multiple switching of the generator voltages. The system described herein operates reasonably well with only the first type of feedback. This feedback regulates the output voltage and improves the wave shape somewhat. However, when the second type feedback is also utilized, the output wave shape is greatly improved and the stability margin is improved, this improvement of the stability margin permitting the first type feedback to be appreciably increased. When the second type feedback is utilized by itself, it effects an appreciable improvement in wave shape although the voltage regulation is not as complete as may be desired. Thus, the combination of both types of feedback give the best overall results.

The second type of feedback is helpful in improving wave shape because it is carrying intelligence to each switching device, i.e., each silicon controlled rectifier. The steep slope of such modulated ripple makes its effect very definitive. The second type feedback is especially helpful in correcting wave shape with a low power factor load.

Thus, with feedbacks as set forth, a sine wave input from the generator and filtering, the needed shaping of

the firing curve for the switching device to produce a sinusoidal power output for a minimum filter size is obtained for any load condition. It is to be noted that using both types of feedback provides the following advantages:

(1) The feedback shapes the output wave to correspond closely to the oscillator wave input, the voltage regulation function being obtained automatically with a response time of much less than a cycle of the power output sine wave.

(2) Since the feedback has in effect provided a linearized amplifier, the power output waveform closely conforms to any input reference oscillator waveform of any frequency up to a fraction of the relatively high generator frequency. With this arrangement, high power square waves, sawtooth waves and other complex waveforms are obtainable.

Referring now back to the modulator depicted in FIG. 5, it is seen that expression

$$\frac{e_1}{+2}+e_3$$

produces the cosine of e_1.

Applied as inputs to D.C. amplifier **102** through resistors **98** and **100** are the signals e_1 and $-e'$ as derived from the computer shown in FIG. 3. Produced at the output of amplifier **102** is the signal $-e_r$ which is the negative voltage across a simulated back to back silicon controlled rectifier pair, e_r being equal to e_1-e'. The signal $-e_I$ is the negative of a voltage proportional to the current from the output of phase e_1 and is the $-ri_1$ signal from the computer in FIG. 3.

To understand the relationship of the circuit of FIG. 5 to the system of FIG. 1, it is to be understood that there is shown in FIG. 5 only a portion of a modulator for mixing one of the generator outputs, for example, the e_1 output with a phase output of the reference voltage oscillator. The portion of the modulator shown in FIG. 5 determines the firing schedule for a back to back pair of switching devices in circuit with the e_1 phase output of the generator. By the term "back to back" pair of switching devices is meant a pair of switching devices where one is switched into conductivity during the positive half of a cycle of a generator output and the other is switched into conductivity during the negative half of such cycle. Thus, the back to back pair of devices, one of which is conveniently designated as R_p, i.e., the device which is switched into conductivity during the positive half cycle of a generator output, and the other of which is designated R_n, i.e., the device which is switched into conductivity during the negative half cycle of the same generator output are suitably in circuit with a generator output such as e_1 to effect such switching. The devices that are simulated are silicon controlled rectifiers.

To provide a single phase output of a system, each modulator, therefore, would include a circuit such as shown in FIG. 5 for each back to back pair of switching devices, the number of each back to back pair of switching devices being determined by the number of balanced phase outputs respectively from the generator. Thus, for each phase of system output, i.e., outputs having the frequency and phases of the outputs reference oscillator, there would be required a modulator, each modulator comprising a number of circuits such as that depicted in FIG. 5, such number being equal to the number of back to back pairs of switching devices in the frequency converter for each stage, i.e., the number of different phase outputs of the generator.

The $-e_M$ signal is supplied to a neutral zone circuit comprising series connected unidirectional potential sources **101** and **103** in shunt with the series connected diodes **105** and **107**, the $-e_M$ signal being applied to the junction **109** of the cathode of diode **107** and the anode of diode **105**. There is taken from the junction **111** of sources **101** and **103**, the signal $-e'_M$.

The signal e_{G1} which is the e_1 output of the computer of FIG. 3 is applied to an input sensing amplifier **108**. Sensing amplifier **108** is suitably an amplifier which normally provides approximately zero volts output when the input thereto is less than zero and a minus voltage, say about -6 volts when the input is equal to or exceeds zero volt. Consequently, amplifier **108** inverts the e_{G1} voltage and the output thereof is a square wave which is at a minus voltage when e_{G1} is positive and at zero volt when e_{G1} is negative. If zero volt at the output of amplifier **108** is taken to be a binary "one," and the minus voltage, such as about -6 volts, is taken to be a binary zero, then the output of amplifier **108** may be designated as the signal $\overline{G}$.

The signal $\overline{G}$ is applied to a logic stage **110** which may be designated a NAND circuit, the latter being the type logic circuit generally used in the circuit of FIG. 5. In the NAND circuit **110**, a zero input thereto provides a minus volts output (binary zero), and a minus volts input thereto provides a zero volt output (binary one). The equations for the function of a NAND circuit may be written as $x=\overline{a}+\overline{b}$, $x=\overline{a}\cdot\overline{b}$ and $\overline{x}=a\cdot b$ wherein x is the output and a and b are inputs. Consequently, the signal $\overline{G}$ at the output of amplifier **108** is inverted in logic circuit **110** to provide the signal G.

The signal $-e'_M$ is applied to a sensing amplifier **104**. Amplifier **104** is a circuit similar to the circuit of stage **108** and which provides a minus volts output when the input thereto is equal to or greater than zero volt and a zero volt output when the input thereto is less than zero volt. In this amplifier, accordingly, only the negative going portion of signal $-e'_M$ is amplified and inverted to provide a signal conveniently designated as M_p which is the basic firing signal for the positive controlled switching device R_p.

The signal $-e'_M$ is also applied to a sensing amplifier **106** wherein the negative portion of the signal $-e_M$ is clipped and only the positively going portion is inverted and amplified to provide the signal conveniently designated as $\overline{M}_n$. The signal $\overline{M}_n$ is inverted in a logic circuit **112** which is a circuit the same as circuit **110**, to provide the signal M_n which is the basic firing signal for the negative controlled switching device. Circuit **106** is one wherein a zero volt output (binary one) is produced when the input thereto is equal to or less than zero volt and a minus volts output (binary zero) is produced when the input thereto exceeds zero volt.

The $-e_r$ signal is applied to an input sensing amplifier **114** similar to that of stages **104** and **108** wherein the negative portion of the signal e_r is clipped and the positive portion is amplified and inverted to provide the signal r. Signal r is inverted in a logic circuit **116** which is the same as the circuits of the other logic stages, such as stages **110** and **112**, to provide the signal $\overline{r}$.

The signals $\overline{G}$, Mn and $\overline{r}$ are applied to a logic circuit **118** to provide at the output thereof the signal $\overline{G}M_n\overline{r}$ and the G, M_p and r signals are applied to a logic circuit **120** to provide at the output thereof the signal $\overline{GM_p}r$.

The $\overline{G}M_n\overline{r}$ signal is applied through a differentiating circuit comprising a series connected capacitor **122** and a parallel connected resistor **124** and thence through the cathode to anode path of a diode **126** to provide sharp negative pulses occurring at the leading edges of the pulses fed into the differentiating circuit, these sharp pulses being applied to an amplifier **128**. The output of amplifier **128** energizes relay R_n which is the negative controlled switching device of the back to back pair of switching devices to effect the closing of normally open contacts R_{n1}.

The $-e_I$ signal which is the $-ri_1$ signal provided from the circuit of FIG. 3 and is the negative of a voltage proportional to the current from the e_1 generator output voltage is applied to a sensing amplifier **130**. Such signal can be applied to sensing amplifier **130** since the

energization of switching device R_n by amplifier **128** has caused normally open contacts R_{n1} associated therewith to close. Sensing amplifier **130** comprises a circuit which provides a binary one output (zero volt) when the input thereto is equal to or less than zero volt and a binary zero output (such as −6 volts) when its input is greater than zero volt. Accordingly, in sensing amplifier **130**, the negative portion of the $-e_r$ signal is clipped and the positive portion is amplified and inverted. The output signal of sensing amplifier **130** may be designated as $\overline{I}_n$ and is negative whenever current flows through switching device R_n. This $\overline{I}_n$ signal when applied to amplifier **128** maintains switching device R_n in its energized state after the negative pulse from diode **126** decays. Switching device R_n becomes deenergized when the current signal $-e_r$ dies out. The latter deenergization occurs before the next negative pulse from diode **126**.

The $\overline{GM_p r}$ signal is differentiated by a series connected capacitor **132** and a parallel connected resistor **134** and the differentiated signals resulting therefrom which comprises a train of sharp negative pulses occurring at the leading edges respectively of the pulses from the output of logic circuit **120** are applied through the cathode to anode path of a diode **136** to a sensing amplifier **138**. Sensing amplifier **138** is a circuit which provides a binary one output (zero volt) when the input thereto is negative and a binary zero output such as −6 volts when the input thereto is equal to or more than zero volt.

It is to be understood that in the signal designation, the term R_n signifies the energized state of the switching device R_n, and the term $\overline{R}_p$ signifies the energized state of switching device R_p.

It is seen that the signal $\overline{GM_p r}$ is the negative of the expression which is required to fire the positive controlled switching device R_p (as will be further explained). Thus the R_p signal is the inversion of $\overline{GM_p r}$ signal. This R_p signal at the output of sensing amplifier **138** is inverted in an amplifier **140** which is a circuit the same as amplifier **128**. The R_p signal which is a binary one or zero volt output causes the deenergization of switching device R_p. Accordingly, when it is so deenergized, the $-e_t$ signal is applied to sensing amplifier **138** through normally closed contacts R_{p1}, the positive portion of the $-e_t$ signal is clipped and the negative portion is amplified and inverted in stage **138**. This positive signal from stage **138** is inverted in amplifier **140** to provide zero output therefrom and relay R_p is held deenergized until the current from the $-e_t$ signal falls to zero.

In FIG. 6 there is shown the arrangement for combining the signals for energizing devices R_n and R_p. It is seen from this figure that when the R_n signal is present, the R_{n1} normally open contacts close and current flows through relay coil R_1 and when the R_p signal is present, R_p is deenergized and the normally closed contacts R_{p1} remain closed and current also flows through relay R_1.

In FIG. 7 there is shown a circuit suitable for use as the sensing amplifiers stages **104**, **108** and **114** of FIG. 5. In this circuit, the input is applied to the base **144** of a PNP transistor **142** through a resistor **146**. Base **144** is connected to a positive pontential source **148** through a resistor **150**, the emitter **152** is connected to ground and the collector **154** is connected to a negative potential source **158** through a resistor **156**. A plurality of outputs may be taken at collector **154**.

Transistor **142** is biased for operation whereby with an input equal to or greater than zero volt applied at base **144**, the output at collector **154** has a minus volts value, suitably about −6.0 volts (a "0"). When the input at base **144** is less than zero volt, the output at collector **154** is about zero volt (a "1").

In FIG. 8, there is shown a circuit suitable for use as the sensing amplifier of stage **106** in FIG. 5. In this circuit, the input is applied through a resistor **160** to the base **164** of a transistor **162**. Base **164** is connected to a source of negative potential **166** through a resistor **168**, and may be connected to a source of positive potential **170** of a chosen value through the anode to cathode path of a diode **173** (shown in dashed lines) whereby the potential at base **164** is positively clamped to the potential from source **170**. The emitter **172** is connected to ground and the collector **174** is connected to a negative potential source **166** through a resistor **176**. A plurality of outputs may be taken at collector **174**.

In the operation of the circuit of FIG. 8, transistor **162** is so biased for operation whereby an input at base **164** having a value of zero volt or a minus voltage provides an approximately zero volt output at collector **174** which may be designated as a binary one. A voltage at base **164** which exceeds zero volt provides a negative voltage output, suitably about −6 volts at collector **174**, such output being conveniently designated as a binary zero.

In FIG. 9, there is shown a circuit suitable for use as the sensing amplifier of stage **138** of FIG. 5. In this circuit the inputs are applied to the base **180** of a PNP transistor **178** through resistors **182** and **184** respectively, base **180** being connected to a source of positive potential **186** through a resistor **188**. The emitter **190** is connected to ground and the collector **192** is connected to a negative potential source **194** through a resistor **196**.

In this circuit, transistor **178** is so biased for operation whereby upon the application of a voltage which has a value less than zero volt to base **180**, an approximately zero volt output is produced at collector **192**, such output being conveniently designated as a binary one. Where the voltage applied to base **180** is equal to or greater than zero, there is produced at collector **192**, a voltage which has a minus value, suitably −6 volts and which may be conveniently referred to as a binary zero. The logic equation for the circuit of FIG. 9 may be described as $x=\overline{a}+\overline{b}$ wherein x is the binary one output and a and b are separate binary zero inputs, the b input actually being an analog quantity where b=1 (binary) when its voltage is equal to or greater than zero volt and b=0 (binary) when it is a negative voltage.

In a circuit of FIG. 10, there is shown a sensing amplifier suitable for use in stage **130** of FIG. 5. In this circuit, the inputs are applied through resistors **206** and **208** to the base **202** of a transistor **198**, base **202** being connected to a source of negative potential **210** through resistor **212**. The emitter **200** is connected to ground and the collector **204** is connected to source **210** through a resistor **214**.

Transistor **198** is so biased for operation whereby when the input to base **202** exceeds zero volt, the output at collector **204** is a negative voltage quantity, such as about −6 volts (binary 0). When the input to base **202** is equal to or less than zero volt, the output at collector **198** is about zero volt, i.e., a binary one. The logic equation for the amplifier of FIG. 10 may be stated as $x=\overline{a}+\overline{b}$. The b voltage input is an analog quantity and may be defined as: b=1 (binary) when its value exceeds zero volt and b=0 (binary) when its value is equal to or less than zero volt.

The circuit of FIG. 11 is suitable for use as a circuit in the logic stages of FIG. 5 such as stages **110**, **112**, etc. Such circuit is conveniently designated as a NAND type which in effect includes an AND function followed by a NOT function or negation. In this circuit, the a and b inputs are applied through resistors **240** and **242** to the base **246** of a transistor **244**, base **246** being connected to a positive potential source **248** through a resistor **250**. The collector **252** is connected to a negative potential source **254** through a resistor **256** and the emitter is connected to ground. The equations for the circuit of FIG. 11 may be stated as output $x=\overline{a}+\overline{b}$, $x=\overline{a}\cdot\overline{b}$ and $\overline{x}=a\cdot b$.

In FIG. 12, there is shown a circuit suitable for use in the amplifier stages **128** and **140** of FIG. 5. In this circuit, the inputs are applied through resistors **224** and **226** to the base **218** of a PNP transistor **216**. The emitter

220 is connected to ground and the collector 222 is connected to a source 228 of negative potential through the switching device being actuated and depicted as a relay coil 230, coil 230 being shunted by the cathode to anode path of a diode 231 to clamp collector 222 at the potential of source 228 and to eliminate inductance surge. The base 218 is connected to a source of positive potential 234 through a resistor 232.

In this circuit, transistor 216 is so biased for operation whereby a negative input to base 218 provides current through coil 230 whereby it is energized. The logic equations in the circuit of FIG. 12 may be written as, $R=\bar{a}+\bar{b}$ and $\bar{R}=a\cdot b$ wherein R signifies the energized state of coil 230 and $\bar{R}$ signifies the deenergized state of coil 230. Utilizing the designation of the signals as shown in connection with amplifier 128 in FIG. 5, then the logic equations for the circuit of FIG. 12 becomes $R_n=\overline{G}M_n\bar{r}+I_nR_n$, since the input to amplifier 128 is $\overline{G}M_n\bar{r}+\bar{I}_n$.

Reference is now made to the circuit of FIG. 5 for an explanation of the operation thereof. It is recalled that the function of this circuit is to provide a schedule for firing switching devices R_n and R_p schematically depicted as relay coils but together behaving as a back to back pair of switching devices such as silicon controlled rectifiers, thyratrons and the like.

The contacts designated R_1 in the circuit of FIG. 2 and the two pairs of contacts R_1 shown at the input at integrator 62 in the circuit of FIG. 3 depict the equivalent of the operation of a back to back switching device pair.

The input signals to the circuit of FIG. 5 as previously explained are received from the circuit of FIG. 3. They are $e_1=e_{G1}$=one generator voltage phase. The term $-e'_M$=the resultant of the mixing of the one phase of the output of oscillator 90 and the cosinusoid of e_1 (in this example, one half voltage e_1 plus e_3), and the providing of two thresholds by clipping out the mid-region of the $-e_M$ signal by the neutral zone circuit. The signal $-e_r$ is the negative of the voltage across a switching device pair where e_r equals e_1-e'. The voltage $-e_I$ is the negative of a voltage proportional to the current from the output phase e_1.

These analog input signals are fed into sensing amplifiers which convert them to on-off, i.e., digital signals. The latter digital signals are mixed and fed through logic amplifiers until the final result is the operation of the output switching device pair (R_n and R_p) in FIG. 5.

As previously explained above, two digital states are described as binary one and binary zero. Binary one signifies the presence of a signal and is a state when the circuit voltage is approximately zero volt. The binary zero state signifies the absence of a signal and exists when the voltage is approximately a suitable negative voltage such as about −6 volts.

The conditions for the operation of switching device R_p which may represent a silicon controlled rectifier having its anode connected to the e_1 generator voltage, i.e., it may represent the positive controlled rectifier in a back to back pair and for the operation of switching device R_n which may represent a silicon controlled rectifier having its cathode connected to the e_1 generator voltage, i.e., it may represent the negative controlled rectifier of the back to back pair are as follows:

Conditions for effecting conduction in positive controlled device R_p

Positive firing signal is present (Derived from input $-e_M$); and	M_p
switching device pair voltage is positive (Derived from $-e_r$; and	r
The generator voltage e_{G1} (same as e_1) is positive; or current i_1 is present and positive (The I_p signal can only be true if the contacts R_{p1} associated with the positive controlled rectifier are closed and current starts to flow (derived from $-e_r$).)	G I_p

Conditions for effecting conduction in negative controlled device R_n

Negative firing signal is present (derived from $-e_M$); and	M_n
Switching device pair voltage is negative (i.e., anode of the negative controlled silicon controlled rectifier woud be positive, derived from $-e_r$); and	$\bar{r}$
The generator voltage e_{G1} is negative (The condition for the negative controlled rectifier to have positive anode voltage); or	$\overline{G}$
Current i_1 is present and negative (The I_n signal is true only after the contacts R_{n1} associated with the negative controlled rectifier are closed and current starts to flow, such current being derived from $-e_I$.)	I_n

Thus, the following equations may be written:

$$R_p=M_prG+I_pR_p \quad (1)$$
$$R_n=M_n\overline{rG}+I_nR_n \quad (2)$$
$$R_1=R_p+R_n \quad (3)$$
$$R_1=M_prG+I_pR_p+M_n\overline{rG}+I_nR_n \quad (4)$$

Equation 4 stands for the proposition that relay R_1 (FIG. 6) is actuated when signals M_p and r and G are concurrently present or have been present (to produce R_p) and I_p is present or the signal M_n is present and concurrently the signals r and g are not present, or this combination has been in existence (to produce R_n) and the signal I_n is present.

In connection with Equation 4, it is to be noted that the I_p and I_n terms do not cause the actuation of relay R_1 since the currents responsible for these terms cannot flow until the relay R_1 is already actuated. Thus, these terms function to hold relay R_1 actuated until the current drops to zero. This is a characteristic inherent in a switching device such as a thyratron or a silicon controlled rectifier R_1 of FIG. 3.

In the circuit of FIG. 5, as has been set forth hereinabove, input voltage e_{G1} may vary widely in frequency but in general is many times greater than the reference voltage frequency from oscillator 90 and consequently, equally many times greater than the output frequency of the system. The e_{G1} signal is amplified and inverted by sensing amplifier 108. Since the voltage to switch amplifier 108 on and off may be chosen to be relatively small, such as about one volt, compared to the magnitude of the e_{G1} voltage, the output of amplifier 108 is essentially a square wave and is negative (binary zero) when voltage e_{G1} is positive and positive (binary one) when voltage e_{G1} is negative. This provides the signal $\overline{G}$ appearing in Equations 2 and 4 above. The $\overline{G}$ signal is inverted in logic circuit 110 to produce the signal G appearing in the Equations 1 and 4.

The input sensing amplifier 106 amplifies and inverts only the positive portion of the $-e'_M$ voltage and its output accordingly becomes $\overline{Mn}$ or the inverse (negative). The $\overline{Mn}$ signal is inverted by logic circuit 112 to produce the Mn signal which is the basic firing angle signal for the negative controlled switching device.

The signal $-e'_M$ is also fed into the sensing amplifier 104 whereby only the negative going portion of the $-e'_M$ signal is amplified. The output of amplifier 104 is the signal M_p which is the basic firing signal for the positive controlled switching device.

The signal $-e_r$, i.e., the voltage across a back to back pair of switching devices is amplified and inverted by sensing amplifier 114 to produce the signal r which is inverted in logic circuit 116 to provide the signal $\bar{r}$.

The signals $\overline{G}$, M_n and $\bar{r}$ are fed into logic circuit 118 to produce the signal $\overline{GM_n\bar{r}}$. From Equation 2 it is seen that this is negative of a term required to actuate the negative controlled switching device.

The differentiating circuit comprising capacitor 122 and

resistor **124** produces short duration negative going pulses at the leading edges of the wider pulses fed into the differentiating circuit. Each of these negative going pulses are amplified in amplifier **128** and the output thereof actuates switching device R_n representing conduction therein. The contacts R_{n1} associated with switching device R_n close upon the energization of device R_n to permit signal $-e_I$ to be fed into sensing amplifier **130**. Since amplifier **130** is biased for operation whereby it only amplifies positive signals, the output of amplifier **130** is the signal $\overline{I}_n$. This signal is negative whenever the negative current is flowing and is the correct polarity to hold the switching device R_n actuated even after the negative pulse from the differentiating circuit decays. After the signal $-e_I$ decays, device R_n becomes deenergized, such deenergization occurring prior to the next pulse from the output of the differentiating circuit.

The signals G, M_p, and r are fed into logic circuit **120**. Its output is according to $\overline{GM_pr}$. This term is the negative of the expression required to fire the positive controlled switching device as shown in Equation 1. The signal $\overline{GM_pr}$ is differentiated in the differentiating circuit comprising capacitor **132** and resistor **134** with the pulses resulting therefrom being applied to sensing amplifier **138**. In amplifier **138**, the pulses are inverted, the output of sensing amplifier **138** being applied to output amplifier **140**, the output of amplifier **140** causing the deenergization of switching device R_p. Thus, the term R_p represents the open or deenergized state of device R_p and term $\overline{R}_p$ represents its actuated state. When switching device R_p is in the deenergized state, the normally closed contacts R_{p1} associated therewith permit the application of the $-e_I$ signal to sensing amplifier **138**. Since this amplifier only senses the negative portion of the signal $-e_I$, such sensing is the correct polarity for the $-e_I$ signal to hold device R_p in the unactuated state until the current drops to zero. The wave shapes of signals at the various points in the circuit of FIG. 5 are shown therein.

In FIGS. 13–16 taken together as in FIG. 17 there is shown a depiction of another embodiment of a system according to the invention wherein silicon controlled rectifiers are utilized as the switching devices to provide frequency conversion. These figures show the details of a modulator for providing one of three phase power outputs from the system, viz., the phase A output. It is, of course, to be realized that modulators similar to those utilized in providing the phase A output are utilized to provide the phase B and phase C outputs.

In FIGS. 13–17, generator **300** provides the outputs e_{G1}, e_{G2} and e_{G3}, these outputs being 120° displaced in phase with respect to each other. The field coil **302** for generator **300** is energized by an exciter **304** which may suitably be of the static type. The three generator outputs are fed back to a voltage regulator contained in stage **304** for providing voltage regulation of the outputs of the generator.

The primary winding **309** of a transformer **310** is connected between the e_{G2} and e_{G3} output lines, the voltage appearing at the upper terminal of a center-tapped secondary winding **311** being applied to summing point **312** through a resistor **314**. The windings of transformer **310** are so poled whereby the waveform appearing at summining point **312** is 90° displaced in phase with respect to the e_{G1} signal, i.e., the e_{G1} cosinusoid which is utilized to establish the firing schedules for the silicon controlled rectifiers associated with the e_{G1} output of generator **300**.

Also, applied to the summing point **312** through a resistor **316** is the phase A output of a three phase sine wave reference oscillator and phase splitter **320**. Oscillator **320** is chosen to have a range of determinable frequencies which is the desired output range of frequencies, the highest frequency of such range being substantially less than the lowest frequency provided from the output of generator **300**. The oscillator output for summing point **312** is taken from the lower terminal of the secondary winding of transformer **320A**.

Also applied to the summing point **312** through a resistor **318** is the phase A system output, such output being applied from an autotransformer **322** to provide analog feedback as an input to the modulator. It is understood that the signal appearing at summing point **312** is utilized to produce the gating signal for the positive controlled silicon controlled rectifier **400** associated with the e_{G1} generator output. By the term "positive controlled" is meant that silicon controlled rectifier **400** is gated into conductivity during a positive half cycle of the e_{G1} generator output.

To provide a similar signal such as that appearing at junction point **312** in order to produce a gating signal for the negative controlled silicon controlled rectifier **404** associated with the e_{G1} generator output, the signal appearing at the lower terminal of secondary winding **311** of transformer **310** is applied to summing point **330** through a resistor **326**. The signal appearing at the polarity dot terminal of the secondary winding of transformer **320A** is applied to point **330** through a resistor **324** and the signal appearing at the undotted terminal of autotransformer **322** is applied to point **330** through a resistor **328**.

It is seen that the signal at summing point **330** is of the opposite polarity as the signal appearing at summing point **312** because of the poling of secondary winding **311**, the poling of the secondary winding of transformer **320A** and the poling of autotransformer **322**.

The signal appearing at junction point **312** is applied to the base **334** of a transistor **332**, transistor **332** having an resistor **[336]** *331*. The base **334** is connceted to positive nected to a source of positive potential **339** through a resistor [**336**] *331*. The base **334** is connected to positive potential source **339** through a resistor **340** and is negatively clamped to ground through the cathode to anode path of a diode **342**. The values of the circuit components associated with transistor **332** are such whereby in the quiescent state, base **334** is positively biased and transistor **332** conducts at saturation but when current into base **334** goes slightly negative, transistor **332** is rendered nonconductive. The output appearing at collector **337** is applied directly to the collector **354** of a transistor **350** as will be further explained hereinbelow.

Applied to the base **345** of a transistor **344** through a resistor **346** is the voltage appearing at the anode **402** of silicon controlled rectifier **400** and also applied to base **345** through a center tapped winding **348** and a resistor **347** is the signal appearing at the cathode **401** of silicon controlled rectifier **400**. In transistor **344**, the collector **349** is connected to the positive source **339** through a resistor **351**, the emitter **353** is connected directly to ground and the base **345** is connected to ground through the cathode to anode path of a diode **355**, diode **355** serving to negatively clamp to ground base **345**. The output appearing at collector **349** is applied to base **352** of transistor **350**.

It has been stated above that the output of collector **337** of transistor **332** is directly applied to collector **354** of transistor **350**. In transistor **350**, the emitter **356** is connected to ground and the base is connected to a negative potential source **358** through a resistor **360**. Also applied to base **352** through a resistor **362** is an output of a reverse current restraining or inhibit circuit **398**, such circuit providing a positive output when current is still flowing in the negative controlled rectifiers as will be further explained hereinbelow.

The output at collector **354** is applied through series connected capacitor **364** to the base **368** of a transistor **366**.

In transistor **366**, the emitter **370** is connected to ground, a series arrangement of resistors **372** and **374** being connected between ground and negative source **358**. The base **368** is connected to the junction **373** of resistors **372** and **374** through the series arrangement of

a feedback winding **376** of a blocking oscillator transformer **378** and a resistor **377**. The collector **380** is connected to positive source **339** through the parallel combination of a winding **379** of transformer **378** and the series arrangement of a resistor **382** and the anode to cathode path of a diode **384**. The upper terminal of winding **381** of transformer **378**, i.e., the polarity dot terminal is connected to the gate electrode **403** of silicon controlled rectifier **400** through a resistor **386** and the lower terminal of winding **381** is connected to the cathode **401** of silicon controlled rectifier **400**.

Considering the operation of that portion of the modulator required to provide the gating signal for silicon controlled rectifier **400**, viz, transistors **332**, **344**, **350**, and **366** and their associated circuit components, the voltage from the reference oscillator applied through resistor **316** to summing point **312** produces a current at the summing point which may suitably be designated as $-I_F$. The cosine timing wave applied through resistor **314** to summing point **312** produces a current thereat which may be suitably designated as $-I_{AC}$. The sum of these two currents analogous to the voltage e_M of FIG. 5, has a similar phase except that it is of the opposite polarity. The analog feedback signal, which contains both the fundamental output frequency and its harmonics and the modulator ripple voltage derived from the multiple switching of the generator voltages and applied to summing point **312** through resistor **318** provides a current, I_0, at summing point **312** in accordance therewith.

Since transistor **332** is arranged to conduct at saturation when its base is substantially at zero volt or slightly higher (0.5 volt) and to be nonconductive at a voltage slightly below zero volt (such as −0.5 volt) a negative signal appearing at summing point **312** renders transistor **332** nonconductive whereby the positive poential appearing at collector **337** is applied to collector **354** of transistor **350**.

In transistor **350**, the negative potential applied to base **352** through resistor **360** provides a negative D.C. threshold. In transistor **344**, to base **345** there are supplied through resistors **346** and **347** respectively, currents in accordance with the signals appearing at the anode **402** and cathode **401** of silicon controlled rectifier **400**. The output at collector **349** of transistor **344** is negative only when e_{G1} output of generator **300** applied to anode **402** of silicon controlled rectifier **400** is positive with respect to cathode **401**. Since the signal appearing at base **345** reflects the difference between the voltages at anode **402** and cathode **401** of silicon controlled rectifier **400**, in the event that such voltage at anode **402** is positive with respect to the voltage on cathode **401**, then transistor **344** is rendered conductive to provide essentially a zero volt output at collector **349**. In the event that the voltage at anode **402** is negative with respect to cathode **401**, then transistor **344** is rendered nonconductive and the output at collector **349** is positive. Accordingly, transistor **344** provides a reverse polarity inhibit feature, such arrangement permitting the gating pulse for silicon controlled rectifier **400** to occur only when the voltage applied to anode **402** is positive. The signal produced at collector **349** of transistor **344** is analogous to the signal $\bar{r}$ produced in the modulator of FIG. 5.

It is seen that in the event the voltage at anode **402** of silicon controlled rectifier **400** is not positive whereby transistor **344** is nonconductive and transistor **350** is consequently heavily conductive, collector **354** of transistor **350** short circuits to ground the output appearing at collector **337** of transistor **332** so that no positive signals can be produced.

Capacitor **364** is included to provide short duration pulses which are produced at the beginning of each pulse period of the signal. Transistor **366** and windings **376**, **379** and **381** provide a blocking oscillator, such blocking oscillator operation being provided by the feedback winding **376**. Diode **384** is included for transient suppression so that an inductance surge will not cause the voltage at collector **380** to exceed breakdown. It is appreciated that in the [evennt] *event* that the output of collector **380** is near zero voltage, then a positive pulse appears at the polarity dot terminal of winding **381** to gate silicon controlled rectifier **400** into conductivity.

The voltage applied from negative source **358** to base **352** through resistor **360** maintains transistor **350** in the nonconductive state when no signal (positive) is present at base **352** of transistor **350**. This permits collector **337** of transistor **332** to go positive when the summing point voltage at base **334** goes negative, thus actuating blocking oscillator transistor **366** to provide output gating pulses. It is realized that the signal on base **334** of transistor **332** and the signal on base **352** of transistor **350** must both be negative to allow the two collectors **337** and **354** (connected together) to go positive and trigger the blocking oscillator. The bias resistor **360** assures that transistor **350** is nonconductive except when either of the aforesaid inputs is positive (NOR circuit).

In FIG.22a, there is shown the compositive wave shape of the currents at summing point **312** comprising A.C. bias current ($-I_{AC}$) superimposed on the reference oscillator current ($-I_f$) and a feedback current proportional to the system output voltage.

The restraining circuit output signal when positive also functions to render transistor **350** conductive whereby the blocking oscillator does not produce output gating pulses. It will be further explained below that a restraining circuit output signal reflects a condition wherein current is still flowing in the negative controlled rectifiers whereby commutation to the positive controlled rectifiers is prevented by such restraining circuit output signal.

In FIG. 22b there is shown the signal observed at collector **337** of transistor **332** when the collector circuit of transistor **350** is opened. FIG. 22c shows the signal appearing at collector **337** of transistor **322** when transistor **350** is connected into the circuit. At first glance, it would appear that the wave shape FIG. 22c should follow the dotted line with the pulse remaining until the controlled rectifier polarity is reversed. However, as soon as silicon controlled rectifier **400** is switched into conductivity, the voltage across it abruptly drops down to a very small figure such as about one volt. The design of the circuit comprising transistor **344** and its associated components is such that with so small a voltage appearing at anode **402** of silicon controlled rectifier **400**, transistor **344** is not rendered conductive and a reverse polarity inhibit signal is produced which causes the wave shape at the output at collector **337** to rapidly drop to zero as soon as silicon controlled rectifier **400** is rendered conductive. If for any reason silicon controlled rectifier **400** is not rendered conductive when it should have been, then the wave shape of the output at collector **337** follows the dotted line of FIG. 22c.

The waveform of FIG. 22d shows the output of the blocking oscillator with its short duration pulse and the waveform of FIG. 22e shows the generator signal e_{G1} (e_{G2} and e_{G3} have the same wave shape), the hatched portions therein indicating when silicon controlled rectifier **400** conducts. It is to be noted that the positive controlled silicon controlled rectifier is essentially being switched into conductivity during the negative half cycle from the reference oscillator output.

The portion of the modulator for providing the gating signals for silicon controlled rectifier **404** which is in back to back relation with silicon controlled rectifier **400**, i.e., it is controlled by the negative half cycles of the e_{G1} output, is the same as that portion for providing the gating signals for silicon controlled rectifier **400**, the polarity of the secondary windings of transformers **310**, **320A** and **322** insuring that the same operation occurs therein. From the waveform of FIG. 22a, it is accordingly seen that a negative controlled silicon controlled rectifier is fired during the positive half cycle of the reference oscillator output.

If the portion of the modulator for providing the firing signals for silicon controlled rectifiers **400** and **404** is considered as a separate unit, then a like pair of units is provided for providing the firing signals for the back to back pair of silicon controlled rectifiers **406** and **408** associated with the generator e_{G2} output and a like pair of units is provided for producing the firing signals for the back to back pair of silicon controlled rectifiers **410** and **412** which are associated with the generator e_{G3} output.

Also, the cosine wave derived from the e_{G2} output is provided from a transformer **308** having a primary winding **305** connected between the e_{G3} and e_{G1} generator output lines, and the cosine wave derived from the e_{G3} output is provided from a transformer **306** wherein the primary winding **301** is connected between the e_{G2} output and the e_{G1} output lines. The upper terminals of the secondary windings **307** and **303** of transformers **308** and **306** are utilized to provide the cosine timing waves for firing positive controlled rectifiers **406** and **410** respectively. The signals appearing at the lower terminals of secondary windings **307** and **303** are utilized as the cosine timing waves for negative controlled silicon controlled rectifiers **408** and **412** respectively.

Likewise, the signal at the lower terminal of the secondary winding of transformer **320A** is utilized to provide the reference voltage for silicon controlled rectifiers **406** and **410** and the signal appearing at the upper terminal of the secondary winding of transformer **320A** is utilized to provide the reference voltage for silicon controlled rectifiers **408** and **412**.

Feedback signals appearing at the lower terminal of winding **322** are utilized to provide the analog feedback for silicon controlled rectifiers **406** and **410** and the signals appearing at the upper terminal of feedback winding **322** are utilized for silicon controlled rectifiers **408** and **412**.

The cathode voltages of the positive bank of silicon controlled rectifiers are respectively applied to the positive controlled silicon controlled rectifier modulator portions through center tapped autotransformer **348** to reverse polarity and the cathode voltages of the negative bank of silicon controlled rectifiers are applied to the modulator portions for negative controlled silicon controlled rectifiers **404**, **408**, and **412** through center tapped windings **414**, **416** and **418**, respectively to reverse polarity.

The cathodes of the positive controlled silicon controlled rectifiers **400**, **406** and **410** are connected to one terminal of an inductor **420** and the anodes of negative controlled rectifiers **404**, **408** and **412** are connected to the other terminal of inductor **420**, inductor **420** serving to combine the outputs of the silicon controlled rectifiers and to filter out substantially most of the harmonics therein.

The output from inductor **420** is filtered across the parallel combination of an inductor **422** and a capacitor **424**. The value of the inductance of inductor **422** is selected to minimize the load current drawn from the system under the worst load and power factor condition. The other parallel combinations, viz, inductor **426** and capacitor **428** and inductor **430** and capacitor **432** respectively are utilized to filter the other combined systems outputs, viz, the phase B output produced by a modulator **450** and a frequency conversion stage **452** comprising silicon controlled rectifiers in circuit with the outputs of generator **300** and the phase C output produced by a modulator **454** and frequency conversion stage **456** comprising silicon controlled rectifiers in circuit with the outputs of generator **300**.

A system phase output, such as the phase A output, also appears in current transformer **460**, current transformer **460** being utilized to provide the restraining signal, for example, which is applied to base **352** of transistor **350** through resistor **362**. The secondary winding **461** of current transformer **460** is center tapped to ground and the upper and lower terminals of secondary winding **461** are connected to bases **472** and **482** of transistors **470** and **480** through resistors **464** and **466**, respectively. In transistor **470**, base **472** is connected to a positive potential source **500**, through a resistor **476**, the collector **474** is connected to positive potential source **500** through a resistor **478** and the emitter **479** is connected directly to ground. In transistor **480**, similarly, base **482** is connected through a resistor **484** to positive potential source **500**, the collector **486** is connected to source **500** through a resistor **488** and the emitter is connected to ground.

The output at collector **486** is applied to those portions of the modulator which are concerned with supplying current restraining signals for the positive controlled silicon controlled rectifiers and the output appearing at collector **474** is applied to those portions of the modulator concerned with providing of current restraining signals for the negative controlled silicon controlled rectifiers.

In the operation of restraining circuit **398**, i.e., current transformer **460** and transistors **470** and **480** and their associated circuit components, transistors **470** and **480** are so biased for operation whereby in the quiescent state, they are slightly positive biased so that the transistors are conducting and the output voltage is substantially zero voltage. Thus, when the current signal from the current transformer crosses the zero point and starts to go negative it overcomes the slight bias and renders the transistors nonconductive.

Let it be assumed that a negative signal appears at the lower terminal of secondary winding **461** of current transformer **460**. In this situation transistor **480** is rendered nonconductive whereby the positive output at collector **486** applied to base **352** of transistor **350** through resistor **362** prevents any gating pulse output from transistor **332** from switching into conductivity silicon controlled rectifier **400** and positive controlled silicon controlled rectifiers **406** and **410** are also similarly restrained.

Similarly, if a negative signal appears at the upper terminal of secondary winding **461** of current transformer **460**, transistor **470** is rendered nonconductive and the positive output appearing at collector **474** is applied as a restraining signal to the modulator portions for the negative controlled silicon controlled rectifiers **404**, **408** and **412** to prevent their being switched into conductivity. A negative signal appearing at the upper terminal of the secondary winding **461** of current transformer **460** indicates that current is still flowing in one or more of the positive controlled silicon controller rectifiers **400**, **406** and **410**. The output at collector **474**, accordingly, prevents commutation to the negative silicon controlled rectifiers **404**, **408** and **412** until the current in transformer **460** passes through the zero point, i.e., when the output of collector **474** is zero. When a negative signal appears in lower terminal of secondary winding **461** of transformer **460**, this signifies that current is still flowing in one or more of the negative controlled silicon controlled rectifiers **404**, **408** and **412** and, similarly, commutation does not occur to the positive silicon controlled rectifiers until the current attains the zero crossover point.

In FIG. 23 there is depicted a logical diagram which corresponds to the modulator shown in FIGS. 13–17. It is seen that the summing of the generator output signal, the reference oscillator output signal, the D.C. bias signal and the feedback signal produces the signal M, the summing of the silicon controlled rectifier anode and cathode voltages produces a signal P_R (or r) and the current in the output provides the restraining signal I_R. The P_R and the I_R inhibit signals are applied to a NOR circuit, the output therefrom being $\overline{P}_R\overline{I}_R$. The AND function to provide the signal $M\overline{P}_R\overline{I}_R$ is not a separate circuit structure but resistor [338] *331* for example, in FIGS. 13–17, which is the common load resistor for collectors **337** and **354** of transistors **332** and **350**, respectively.

With regard to the output filter, the tuned filter as

shown therein is a very satisfactory means for providing a faithful sinusoidal output. However, a tuned circuit is not strictly necessary since the size of the capacitor therein has to be determined at maximum load and for adequate filtering. At such maximum load level, the "Q" of the circuit is very low and the circuit is detuned by the load. At light loads, it becomes unnecessary to have a tuned parallel filter since the capacitor is large enough to provide excellent filtering without the inductive member of the parallel combination.

The system of this invention[, namely, a system for providing a plurality of balanced phased outputs, having a range of determinable frequencies from a generator having such plurality of balanced phase outputs, the system output having a frequency which is less than the lowest frequency of the generator outputs,] may be paralleled with like polyphase output systems. In the event that paralleling is made between like systems of this invention, there would be included therein real and reactive load divisions circuits such as are well known in the art. The reactive load division circuits are utilized to sense the reactive component of current and the signal produced therefrom is utilized to increase the output voltage of one of the systems in the parallel arrangement depending upon whether such system is carrying less than or more than its share of the reactive load.

The real load division signal is essentially used to increase or decrease the frequency of the system being controlled depending upon whether such system is carrying less than or more than its share of the real load. Actually, the parallel arrangement of systems have to remain at the same frequency as long as they are in synchronism. The real load division signal is utilized to increase or decrease the frequency of the output from the reference oscillator.

It is well known in the art to have protective circuits for sensing over and undervoltages, over and underfrequencies and differential faults. It is contemplated in accordance with this invention to utilize circuits for providing protective functions in conjunction with the system of the invention.

While there have been shown particular embodiments of this invention, it will, of course, be understood that it is not wished to be limited thereto since different modifications may be made both in the circut arrangements and in the instrumentalities employed and it is contemplated in the appended claims to cover any such modifications as fall within the true spirit and scope of the invention.

What is claimed as new and desired to be secured by Letters Patent of the United States is:

[1. In combination with a varying frequency power source having a chosen plurality of like balanced phase outputs, said chosen plurality of frequency conversion means, each of said conversion means comprising said chosen plurality of first and second silicon controlled rectifiers, each of said silicon controlled rectifiers comprising an anode, a cathode and a gate electrode, the anode of each of said first silicon controlled rectifiers respectively being coupled to one of said power source outputs, the cathode of each of said second silicon controlled rectifiers respectively being connected to one of said power source outputs; a reference voltage source having said chosen plurality of balanced phase outputs, the frequency of said reference voltage being less than the lowest frequency of the outputs from said power source, said chosen plurality of modulating means, each of said modulating means being in circuit with the outputs of said power source and one of the outputs of said reference voltage source for mixing said power source outputs with said reference voltage, means for applying the respective outputs of said modulating means to the gate electrodes of said silicon controlled rectifiers comprising corresponding ones of said frequency conversion means, and said chosen plurality of means for respectively combining the outputs of the silicon controlled rectifiers included in each of said frequency conversion means to provide said chosen plurality of balanced phase system outputs, the cathodes of said first rectifiers and the anodes of said second rectifiers being connected to said combining means, each of said last named outputs having the frequency of said reference voltage, said first silicon controlled rectifiers being conductive during the coincidence of half cycles of said power source outputs and half cycles of said combining means output of one polarity, said second silicon controlled rectifiers being conductive during the coincidence of half cycles of power source outputs and half cycles of said combining means outputs and of the opposite polarity.]

2. In combination with a varying frequency power source having a chosen plurality of like balanced phase outputs, said chosen plurality of frequency conversion means, each of said conversion means comprising said chosen plurality of first and second silicon controlled rectifiers, each of said silicon controlled rectifiers comprising an anode, a cathode and a gate electrode, the anode of each of said first silicon controlled rectifiers respectively being coupled to one of said power source outputs, the cathode of each of said second silicon controlled rectifiers respectively being connected to one of said power source outputs, a reference voltage source having said chosen plurality of balanced phase outputs, the frequency of said reference voltage being less than the lowest frequency of the outputs from said power source, said chosen plurality of modulating means, each of said modulating means being in circuit with the outputs of said power source and one of the outputs of said reference voltage source for mixing said power source outputs with said reference voltage, means for applying the respective outputs of said modulating means to the gate electrodes of said silicon controlled rectifiers comprising corresponding ones of said frequency conversion means, said chosen plurality of means for respectively combining the outputs of the silicon controlled rectifiers included in each of said frequency conversion means to provide said chosen plurality of balanced phase system outputs, the cathodes of said first rectifiers and the anodes of said second rectifiers being connected to said combining means, each of said last named outputs having the frequency of said reference voltage, said first silicon controlled rectifiers being conductive during the coincidence of half cycles of said power source outputs and half cycles of said combining means output of one polarity, said second silicon controlled rectifiers being conductive during the coincidence of half cycles of power source outputs and half cycles of said combining means outputs and of the opposite polarity and said chosen plurality of means for directly feeding back the output of each combining means respectively to a corresponding modulating means.

3. In combination with a varying frequency power source having a chosen plurality of like balanced phase outputs, said chosen plurality of frequency conversion means, each of said frequency conversion means comprising said chosen plurality of first and second silicon controlled rectifiers, each of said silicon controlled rectifiers respectively comprising an anode, a cathode, and a gate electrode, the anode of each of said first silicon controlled rectifiers being respectively coupled to one of said power source outputs, the cathode[s] of each of said second silicon controlled rectifiers being coupled respectively to one of said power source outputs, a reference voltage source having said chosen plurality of balanced phase outputs, the frequency of said reference voltage being less than the lowest frequency of the outputs from said power source, said chosen plurality of modulating means, each of said modulating means being in circuit with the outputs of said power source and one of the outputs of said reference voltage source for mixing said power source outputs with said reference voltage, means for applying the respective outputs of said modulating means to the gate electrodes of the silicon controlled rectifiers comprising cor-

responding ones of said frequency conversion means, said chosen plurality of means for respectively combining the outputs of the silicon controlled rectifiers included in each of said frequency conversion means to provide said chosen plurality of balanced phase system outputs, each of said last named outputs having the frequency of said reference voltage, the cathodes of said first rectifiers and the anodes of said second rectifiers being connected to said combining means, said first silicon controlled rectifiers being conductive during the coincidence of half cycles of said power source outputs and half cycles of said combining means outputs of one polarity, said second silicon controlled rectifiers being conductive during the coincidence of half cycles of said power source outputs and said combining means outputs of the opposite polarity, said chosen plurality of means for directly feeding back the output of each combining means to a corresponding modulating means, and said chosen plurality of means responsive to the current of said respective combining means outputs for preventing the switching into conductivity of one of said plurality of silicon controlled rectifiers while current is still flowing in the other plurality of said silicon controlled rectifiers.

4. In combination with a varying frequency power source having a chosen plurality of like balanced phase outputs, said chosen plurality of frequency conversion means, each of said conversion means comprising said plurality of first and second silicon controlled rectifiers, each of said silicon controlled rectifiers comprising an anode, a cathode, and a gate electrode, the anode of each of said first silicon controlled rectifiers respectively being coupled to one of said power source outputs, the cathode[s] of each of said second silicon controlled recifiers respectively being coupled to one of said power source outputs, a reference voltage source having said chosen plurality of balanced phase outputs, the frequency of said reference voltage being less than the lowest frequency of the outputs of said power source, said chosen plurality of modulating means, each of said modulating means being in circuit with the outputs of said power source and one of the outputs of said reference voltage source for mixing said power source outputs with said reference voltage, means for applying the respective outputs of said modulating means to the gate electrodes of the silicon controlled rectifiers comprising corresponding one of said frequency conversion means, said chosen plurality of means for respectively combining the outputs of the silicon controlled rectifiers included in each of said frequency conversion means to provide said chosen plurality of balanced phase system outputs, each of said last named outputs having the frequency of said reference voltage, the cathodes of said first rectifiers and the anodes of said second rectifiers being connected to said combining means, said first silicon controlled rectifiers being conductive during the coincidence of half cycles of said power source output and half cycles of said combining means outputs of one polarity, said second silicon controlled rectifiers being conductive during the coincidence of half cycles of said power source outputs and half cycles of said combining means outputs and of the opposite polarity, filter means coupled to the outputs of said combining means for removing from said combined outputs those components having frequencies other than the frequency of said reference voltage, said chosen plurality of *inhibit* means responsive to the respective currents in said combined outputs for preventing the switching into conductivity of one plurality of silicon controlled rectifiers while current is still flowing in the other plurality of said silicon controlled rectifiers, and said chosen plurality of means for directly feeding back the output of a combining means to a corresponding modulating means respectively.

5. In the combination defined in claim **4** wherein said power source outputs are sinusoidal waves and wherein means are further included for converting said sinusoidal waves to corresponding cosinusoidal waves, said cosinusoidal waves being mixed with said reference voltage.

6. In the combination defined in claim **5** wherein each modulating means includes first and second of said chosen pluralities of mixing units, each of said first plurality of mixing units being respectively in circuit with a different cosinusoidal power source output in a first given polarity, in circuit with the reference voltage in a chosen polarity, and with the output of said feedback means in a predetermined polarity, a mixing unit including means for summing said cosinusodial power source output, said reference voltage source output and said feedback means output, the resultant of said summing being applied as a switching signal to the gate electrode of an associated first silicon controlled rectifier, each of said second units being respectively in circuit with a different cosinusoidal power source output, said reference voltage source output and said feedback means output and in polarities opposite to the polarities in a first unit, each of said second units including means for summing said different cosinusoidal power source output, said reference voltage source output and said feedback means output, the resultant of said last named summing being applied as said switching signal to the gate electrode of an associated second silicon controller rectifier.

7. In the combination defined in claim **6** wherein each of said units further comprises means for summing the voltages appearing at the anode and cathode of an associated silicon controlled rectifier and means responsive to sum of said voltages for enabling the application of said switching signal to said associated silicon controlled rectifier only when the voltage at said anode exceeds the voltage at said cathode.

8. In the combination defined in claim **7** wherein there is further included a threshold voltage source and means for comparing said switching signal with said threshold voltage, said silicon controlled rectifier being switched into conductivity only when said switching signal voltage exceeds said threshold voltage.

9. In the combination defined in claim **8** wherein each mixing unit includes means for combining the voltage resulting from the summing of said anode and cathode voltages, said threshold voltage and the voltage produced from said preventing means, means for comparing said switching signal with the output of said last named combining means, said associated silicon controlled rectifier being switched into conductivity only when said switching signal voltage exceeds the voltage from said last named combining means.

10. In the combination defined in claim **9** wherein each mixing unit further includes a blocking oscillator having applied thereto the output of said comparing means, the output of said blocking oscillator being applied as switching signals to the gate electrode of the associated silicon controlled rectifier.

11. In the combination defined in claim **10** wherein said [preventing] *inhibit* means includes a current transformer responsive to the current in the output of a combining means, a first transistor amplifier responsive to current flowing in said second plurality of silicon controlled rectifiers to produce an output for preventing switching signals from being applied to said first plurality of silicon controlled rectifiers and a second transistor amplifier responsive to current flowing in said first plurality of silicon controlled rectifiers to produce an output for preventing switching signals from being applied to said second plurality of silicon controlled rectifiers.

12. A frequency conversion system comprising a power source producing an indeterminate frequency, a first group of switching devices coupled to said power source, each switching device of said first group being actuated into conductivity by switching signals being applied thereto when said switching device is enabled by the output from said power source of one polarity, a second group of

switching devices coupled to said power source, each switching device of said second group being actuated into conductivity by switching signals being applied thereto when said switching device is enabled by the output from said power source of the opposite polarity, a reference frequency source, the frequency of said reference frequency source being less than the lowest frequency of said power source, modulating means coupled to said power source and to said reference frequency source, said modulating means including a number of control means, each control means being coupled to a corresponding one of said switching devices to supply said switching signals thereto at times controlled by the combined outputs of said power source and said reference frequency source, combining means coupled to said switching devices to combine the outputs thereof to produce a power output having the frequency of said reference frequency source and means for directly feeding back the power output from said combining means to each of said control means to combine said power output with the outputs of said power source and said reference frequency source to further control the times at which said switching signals are applied to said switching devices.

13. A frequency conversion system comprising a power source producing a number of balanced phase outputs of an indeterminate varying frequency, at least one frequency conversion means, each frequency conversion means comprising first and second groups of switching devices, each switching device of said first group being actuated into conductivity by switching signals being applied thereto when said switching device is enabled by the associated phase output from said power source of one polarity, each switching device of said second group being actuated into conductivity by switching signals being applied thereto when said switching device is enabled by the associated phase output from said power source of the opposite polarity, a reference frequency source producing a number of phase displaced outputs equal to the number of frequency conversion means, the frequency of said reference frequency source being less than the lowest frequency of said power source, combining means coupled to each frequency conversion means to combine the outputs of the switching devices therein to produce a number of balanced phase outputs equal to the number of frequency conversion means and having the frequency of said reference frequency source, modulating means equal in number to the number of frequency conversion means, each modulating means being coupled to an associated frequency conversion means, said modulating means each including a number of control means equal to the number of switching devices within the associated frequency conversion means, each of said control means being coupled to one of said power source outputs, the associated output from said reference frequency source and to the output of the combining means for the associated frequency conversion means, each control means being actuated to produce said switching signals at times controlled by the three last-named outputs, and means coupling the switching signals from each control means to the corresponding switching device in said associated frequency conversion means.

14. A frequency conversion system as recited in claim 13 wherein each of said control means includes summing means for combining the outputs from said power source, said reference frequency source and said combining means to produce control signals and tarnsistor switche means producing said switching signals when triggered by said control signals.

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