

(19) World Intellectual Property Organization
International Bureau



(43) International Publication Date
7 May 2009 (07.05.2009)

PCT

(10) International Publication Number
WO 2009/056500 A2

(51) International Patent Classification:
H04L 25/03 (2006.01) *H04L 25/02* (2006.01)

(74) Agent: PAGE WHITE & FARRER; Bedford House,
John Street, London Greater London WC1N 2BF (GB).

(21) International Application Number:
PCT/EP2008/064464

(81) Designated States (*unless otherwise indicated, for every kind of national protection available*): AE, AG, AL, AM, AO, AT, AU, AZ, BA, BB, BG, BH, BR, BW, BY, BZ, CA, CH, CN, CO, CR, CU, CZ, DE, DK, DM, DO, DZ, EC, EE, EG, ES, FI, GB, GD, GE, GH, GM, GT, HN, HR, HU, ID, IL, IN, IS, JP, KE, KG, KM, KN, KP, KR, KZ, LA, LC, LK, LR, LS, LT, LU, LY, MA, MD, ME, MG, MK, MN, MW, MX, MY, MZ, NA, NG, NI, NO, NZ, OM, PG, PH, PL, PT, RO, RS, RU, SC, SD, SE, SG, SK, SL, SM, ST, SV, SY, TJ, TM, TN, TR, TT, TZ, UA, UG, US, UZ, VC, VN, ZA, ZM, ZW.

(22) International Filing Date: 24 October 2008 (24.10.2008)

(25) Filing Language: English

(26) Publication Language: English

(30) Priority Data:
0721426.5 31 October 2007 (31.10.2007) GB

(71) Applicant (*for all designated States except US*): ICERA INC [US/US]; Corporation Trust Center, 1209 Orange Street, Wilmington, New Castle, Delaware (US).

(84) Designated States (*unless otherwise indicated, for every kind of regional protection available*): ARIPO (BW, GH, GM, KE, LS, MW, MZ, NA, SD, SL, SZ, TZ, UG, ZM, ZW), Eurasian (AM, AZ, BY, KG, KZ, MD, RU, TJ, TM), European (AT, BE, BG, CH, CY, CZ, DE, DK, EE, ES, FI, FR, GB, GR, HR, HU, IE, IS, IT, LT, LU, LV, MC, MT, NL, NO, PL, PT, RO, SE, SI, SK, TR), OAPI (BF, BJ, CF, CG, CI, CM, GA, GN, GQ, GW, ML, MR, NE, SN, TD, TG).

(72) Inventors; and

(75) Inventors/Applicants (*for US only*): LUSCHI, Carlo [IT/GB]; 7 Marlborough Court, Duke Street, Oxford OX2 0QT (GB). WALKER, Simon [GB/GB]; 4 Heathermount Drive, Crowthorn, Berkshire RG45 6HN (GB). ALL-PRESS, Steve [GB/GB]; 36 Canynge Square, Clifton, Bristol BS8 3LB (GB). JONES, Philip [GB/GB]; 4 The Green, Wooton Bassett, Swindon Wiltshire SN4 8ND (GB).

Published:

— *without international search report and to be republished upon receipt of that report*



WO 2009/056500 A2

(54) Title: A RADIO RECEIVER IN A WIRELESS COMMUNICATIONS SYSTEM

(57) Abstract: A radio receiver and corresponding method for a wireless communications system. The receiver comprises: channel equalisation means arranged to receive samples of an incoming signal and to generate an equalised output, the channel equalisation means comprising means for processing the digital samples in accordance with an equaliser algorithm. The receiver further comprises: means for estimating parameters of a channel over which the incoming signal has been transmitted, and means for selecting from a plurality of equaliser algorithms an equaliser algorithm for execution by the processing means based on at least one of the estimated channel parameters.

A RADIO RECEIVER IN A WIRELESS COMMUNICATIONS SYSTEM

The present invention relates to a radio receiver in a wireless communications system, and to a method of processing radio signals.

5

The transmission of radio signals carrying data in modern wireless communications can be realized based on a number of different communications systems, often specified by a standard. There are increasing requirements for devices which are able to operate to support more than one of these wireless communications systems. Mobile radio receiver devices include analog radio frequency (RF)/intermediate frequency (IF) stages, which are arranged to receive and transmit wireless signals via one or more antennas. The output of the RF/IF stages is typically converted to baseband, where an Analog-to-Digital Converter (ADC) converts incoming analog signals to digital samples, which are then processed for signal detection and decoding of the data in the form of logical values. The ADC may alternatively operate directly at IF, in which case the conversion to baseband is performed in the digital domain. A number of different types of front end processing of the digital samples are known to implement signal detection, including rake receiver processing and channel equalisation processing.

20

In Code Division Multiple Access (CDMA) wireless systems, different physical channels are multiplexed in the code domain using separate spreading sequences. In the case of orthogonal spreading codewords, the original data symbols can then be effectively separated at the receiver by despreading.

25

In a Wideband CDMA (WCDMA) cellular system, downlink code multiplexing is performed using Orthogonal Variable Spreading Factor (OVSF) codes. However, the OVSF codewords are orthogonal to each other only under the condition of perfect time alignment. In the presence of multipath propagation, the code orthogonality is lost, and the operation of despreading is affected by Multiple Access Interference (MAI).

30

CDMA mobile radio receivers conventionally employ a rake processor which relies on the correlation properties of the spreading sequences. A rake processor is

described for example in J. G. Proakis, "Digital Communication", New York, McGraw-Hill, 1995. This type of receiver is subject to performance degradation in the presence of code correlation, if the MAI between code-multiplexed transmission is comparable to the other sources of noise and interference. Under
5 these conditions, a performance advantage may be achieved by attempting to restore the orthogonality between the codes before despreading. The sub-optimality of conventional 3GPP receivers based on rake processing causes a significant performance penalty, especially for downlink data rates increasing from the 384 kbps for WCDMA Release 99 to High Speed Downlink Packet Access
10 (HSDPA) rates of several Mbps. When the code orthogonality is destroyed by multipath, an effective approach is to use channel equalisation instead of rake processing.

Channel equalisation techniques have been widely employed over the last
15 decades for combating intersymbol interference on frequency selective transmission channels. Channel equalization techniques are described in J. G. Proakis, "Digital Communication", New York, McGraw-Hill, 1995, and S. Benedetto, E. Biglieri, and V. Castellani, "Digital Transmission Theory", Englewood Cliffs, NJ, Prentice-Hall, 1987. Channel equalisers have recently found application
20 in receivers for Time Division Multiple Access (TDMA) and Code Division Multiple Access (CDMA) mobile wireless systems. An example of application of channel equalisation to a CDMA cellular system is described in A. Klein "Data Detection Algorithms Specially Designed for the Downlink of CDMA Mobile Radio Systems", in Proceedings of IEEE Vehicular Technology Conference, vol. 1, Phoenix, AZ,
25 May 1997, pp. 203-207. In particular in synchronous CDMA cellular systems, as in the case of the forward link of the 3GPP WCDMA standard, chip level equalisation allows to significantly improve the performance over conventional rake receivers, at the cost of an increased implementation complexity. This advantage is especially important for high rate data transmission, as in 3GPP high
30 speed downlink packet access (HSDPA).

It is an aim of the present invention to optimise the processing facilities of a receiver in a wireless communication environment, in particular taking into account

processing performance set against the computing resources and/or power consumption required to obtain that processing performance.

5 According to the present invention there is provided a radio receiver for a wireless communications system comprising: channel equalisation means arranged to receive samples of an incoming signal and to generate an equalised output, said channel equalisation means comprising means for processing said digital samples in accordance with an equaliser algorithm; means for estimating parameters of a channel over which the incoming signal has been transmitted; and means for
10 selecting from a plurality of equaliser algorithms an equaliser algorithm for execution by the processing means based on at least one said estimated channel parameter.

Another aspect of the present invention provides a method of processing radio
15 communication signals in a radio receiver, the method comprising: receiving digital samples of an incoming radio communication signal and processing those samples in accordance with an equaliser algorithm; estimating at least one parameter of a channel over which the incoming signal has been transmitted; and selecting said equaliser algorithm from a plurality of equaliser algorithms based on
20 at least one said estimated channel parameter.

In the described embodiment, the step of selecting said equaliser algorithm comprises: selecting between a linear and a non-linear structure; selecting
25 between a Baud-spaced and a fractionally-spaced structure; and selecting one of a plurality of different equaliser cost functions. The method can comprise the additional step of selecting between equaliser block processing and implementation of a tap adaptation rule. The selection between these two may be made dependent on a channel parameter representative of channel mobility. In this context, channel mobility can mean channel non-stationarity or temporal
30 selectivity, and can be achieved for example through an estimate of a channel Doppler spread.

A computer program product is also provided which implements the method defined above when executed on a processor. In this case, the processor can

constitute the same processing means as the one that executes the equaliser algorithms themselves. That is, the program for selecting one of a plurality of equaliser algorithms can be executed by the same processor that executes the algorithms themselves to implement an equaliser function.

5

The inventors have realised that the extent to which channel equalisation can provide an optimised trade-off between superior performance and use of the available processing resources and/or power consumption is dependent on certain channel conditions. More particularly, the inventors have appreciated that the particular equalisation algorithm which is used to implement the channel equalisation can provide different benefits in dependence on certain channel conditions.

The inventors have further appreciated that the parameters selected for implementing the particular equalisation algorithm can further enhance performance if selected based on certain channel conditions.

In this context, the word channel is used to denote the communication path of the radio signals. According to the communication system used, channels can be defined by time, code or frequency, as is well known in the art. The quality of particular channels is affected by conditions related to the propagation environment, the cellular layout and other conditions in the wireless communications system.

For a better understanding of the present invention and to show how the same may be carried into effect, reference will now be made by way of example to the accompanying drawings in which:

Figure 1 is a schematic block diagram of a wireless communications device;

Figure 2 is a block diagram showing selection between rake receiver processing and equaliser processing;

Figure 3 is a schematic block diagram of processing functions;

Figure 4 is a schematic diagram of a sequence of steps for selecting a processing function;

Figure 5 is a schematic block diagram for the selection of a set of equaliser parameters; and

Figure 6 is a schematic block diagram for the selection of the equaliser algorithm.

5

Figure 1 is a schematic block diagram of a device for transmitting and receiving signals in a wireless communications system. Such a device can be implemented in a number of different ways, but in accordance with Figure 1 a series of RF/IF stages 32 is arranged to receive and transmit wireless signals (TX, RX) via one or more antennas 20. The embodiments of the present invention discussed herein are principally concerned with receiving wireless signals, and so that transmit signals will not be mentioned further. The received signal at the output of the RF/IF stages is typically converted to baseband, where an ADC converts the analog signal into digital samples. The block 32 of Figure 1 includes components for processing the received radio signals and providing digital signal samples $r(k)$. This can be achieved in different ways, which are known in the art and which are not discussed further herein.

The samples $r(k)$ are supplied to a data transfer engine 30 which communicates with a processor 22, an instruction memory 24 and a data memory 26. The processor 22 is responsible for processing the samples $r(k)$. The processor 22 can execute a number of different functions which are held in an instruction memory 24 in the form of code sequences. This provides a so-called soft modem which has a number of advantages discussed further herein.

25

Figure 2 and Figure 3 are schematic block diagrams which illustrate some among a number of different functions that are executed by the processor 22. A first function denoted by block 10 is referred to as estimation of channel parameters. This function estimates a number of different parameters related to the communication channels over which the radio signals are transmitted in the wireless communication system. The function 10 provides at time k the outputs $\gamma_n(k)$, $n=1, \dots, N_C$, where N_C denotes the number of estimated channel parameters, that represent a set of channel parameters derived from the received

30

signal samples $r(k)$. The estimated channel parameters $\gamma_n(k)$ can be used for a number of different purposes. As illustrated in Figure 2 and Figure 3, they are supplied to a *Selection of Rake/Equaliser Receiver* function 12 which determines whether to process the received samples using a rake receiver or an equaliser receiver. The rake receiver or equaliser receiver is implemented by the processor 22 executing the appropriate code sequence from the instruction memory 24.

The parameters $\gamma_n(k)$ are further supplied to a *Selection of Equaliser Algorithm* function 18 which is used in the event that an equaliser receiver 16 is selected. If used, the function 18 selects a particular algorithm for implementing the equaliser receiver 16 based on the channel parameters which have been estimated. The algorithm is supplied to the channel equaliser as denoted diagrammatically by input 17. In practice of course this will be implemented by the appropriate algorithm being selected as a code sequence from the instruction memory.

The channel parameters $\gamma_n(k)$ are also supplied to a *Selection of Equaliser Parameters* function 14. The equaliser parameter selection function 14 is used in the event that an equaliser receiver is selected (as denoted by block 16) and controls parameters used for implementing the equaliser receiver, these parameters being denoted $\theta_n(k)$, $n = 1, \dots, N_E$, where N_E denotes the number of relevant equaliser parameters.

The use of the estimated channel parameters to control the selection of a rake receiver or equaliser receiver (function 12) will now be discussed in more detail. Figure 2 illustrates the concept in schematic form. The digital samples $r(k)$ are supplied to a switch 4 which has an input 5 receiving the command signal for the selection of rake receiver or equaliser processing from the function 12. In accordance with this signal, the switch 4 selects a processing path 6 via a rake receiver 7, or a processing path 8 via an equaliser 9. As is known in the art, the rake receiver includes a set of rake fingers 7a, 7b, ... , for each channel transmitted on a separate channelization code. Each finger is associated with a single descrambler/despreader 9 and a weighting function 11, and the set of fingers relative to each channel are associated to an adder 13 providing a

processed output on output path 15. As the operation of a rake receiver is well understood to a person skilled in the art, its function will not further be described here.

5 The equaliser receiver 19 comprises a chip level equaliser 16 and a plurality of descramblers/depreaders 21a, 21b, ... for each channel transmitted on a separate channelization code. The outputs of the descramblers/despreaders are supplied along output path 23. An output switch 25 provides processed outputs on lines 27 to subsequent decoding functions. The switch 25 is (like the switch 4) controlled
10 by control input 5 which receives the command signal for the selection of rake receiver or equaliser from the function 12.

While Figure 2 illustrates the concept of processing function selection, it will readily be appreciated that in the embodiment of the invention illustrated in Figure 1 it is
15 not possible to identify different physical paths (6, 8, 15, 23). Instead, selection is made by downloading different code sequences dependent on whether a rake receiver function or equaliser receiver function is to be executed by the processor 22.

20 In such a software implementation of the receiver, where only either rake or equaliser processing is performed at any given time, the above approach also provides an overall reduction of computational complexity with respect to a conventional receiver implementing a channel equaliser in hardware. In this respect conventional modems based on a hardware implementation are forced to
25 the choice between a design dictated by the maximum data rate requirements and the instantiation of multiple algorithms as separate areas of silicon. These solutions imply higher implementation costs, size and/or power consumption and any compromise would inevitably penalise performance. On the other hand, the proposed solution allows to reduce complexity, size and cost by reusing a
30 common platform to adaptively select the optimum set of signal processing functions capable of maximising performance and minimise power consumption.

Reference will now be made to Figure 4 to describe a method of selecting a processing function based on the estimation of particular channel parameters.

The inventors have found that it is advantageous to apply the selection criteria by examining different channel parameters in a certain sequence (as illustrated in Figure 4 and described below). It will readily be appreciated however that other appropriate sequences may also be utilised.

5

Step S1 produces an estimate of the degree of non-stationarity of the channel, related to mobility of the user of the transmission channel, given for example by an estimate of the Doppler spread or the maximum Doppler frequency or by an estimate of the relative speed of the mobile terminal. These estimators are known
10 in the art and so the manner in which it is estimated is not discussed further herein. Examples are described in G. L. Stuber, "Principles of Mobile Communications", Norwell, MA, Kluwer, 1996, A. Sampath and J. M. Holtzman, "Estimation of Maximum Doppler Frequency for Handoff Decisions", in Proceedings of IEEE Vehicular Technology Conference, Secaucus, NJ, May 1993,
15 pp. 859-862, C. Tepedelenlioglu, A. Abdi, G. B. Giannakis, and M. Kaveh, "Estimation of Doppler spread and Signal Strength in Mobile Communications with Applications to Handoff and Adaptive Transmission", Wireless Communications and Mobile Computing, vol. 1, no. 2, pp. 221-242, March 2001, and references therein. The receiver can be designed to use equaliser processing for relatively
20 low time-varying channels, and to switch to rake processing for fast time-varying channels, where the switching threshold should depend on the desired trade-off between equaliser complexity and receiver performance. A *Doppler comparison* step S2 compares a Doppler estimation signal γ_1 with a suitable threshold Th_d . If γ_1 exceeds the threshold Th_d , the step selects rake receiver processing. If the
25 Doppler estimation signal γ_1 does not exceed the threshold Th_d , the comparison produces a negative answer, and the selection process continues with an *out-of-window energy comparison* step.

The out-of-window energy estimation S3 provides an estimate of the channel
30 energy outside the time window used for equaliser channel estimation. An example is described in C. Luschi, M. Sandell, P. Strauch, and R.-H. Yan, "Adaptive Channel Memory Truncation for Digital Mobile Communications", in Proceedings of IEEE International Workshop on Intelligent Signal Processing and

Communication Systems, Melbourne, Australia, November 1998, pp. 665-669. Equaliser processing is selected only when a significant percentage of the channel energy is captured by the channel estimation window – which will not happen in the case of very high delay spread). To this end, the out-of-window energy γ_2 is compared with a threshold Th_w . If γ_2 is greater than the threshold Th_w , the step selects rake receiver processing. If the out-of-window energy γ_2 is not greater than Th_w , to the selection process continues with a *single-ray channel detection* step.

10 A delay spread estimation S5 generates an output γ_3 , given for example by an estimate of the root mean square (rms) delay spread. An example of delay spread estimation is given in H. Arslan and T. Yucek, "Delay Spread Estimation for Wireless Communication System", in Proceedings of IEEE International Symposium on Computers and Communication, Kemer-Antalya, Turkey, June-July 15 2003, pp. 282-287. The parameter γ_3 is supplied to the *single-ray channel detection* step S6 to determine if the transmission channel can be considered to result from a single propagation path (multipath absent). In case of single-path propagation, the step selects rake receiver processing.

20 More generally identification of the conditions of very high delay spread (long channel impulse response) and zero delay spread (single ray channel impulse response) can be used to switch the receiver to rake receiver processing. The term "channel length" is often used in the art to denote the temporal duration of the channel impulse response, which is related to the channel delay spread.

25 In the event of non single-ray channel, the process passes to an estimate of channel characteristics from the location of the channel zeros in the z-plane (S7). Examples of how this is done are given in Y. Bistritz, "Zero Location with Respect to the Unit Circle of Discrete-Time Linear System Polynomials", Proceedings of the 30 IEEE, vol. 72, no. 9, pp. 1131-1142, September 1984, and references therein. The receiver may be designed to switch to rake processing in the presence of locations of the zeros that identify channel characteristics that are critical for the operation of the equaliser - as in the case of linear equalisation with channel zeros

close to the unit circle of the z-plane, or for fractionally-spaced equalisation or, more generally receive diversity equalisation (multiple receive antennas or multiple subchannels obtained by oversampling) with common zeros among the equaliser subchannels. The estimate of the channel zeros location γ_4 is supplied to a
5 critical zeros location detector step S8, which selects rake receiver processing in the presence of the locations of zeros which would be critical for operation of an equaliser. In case of non-critical channel characteristics, the selection process continues with a *cell geometry comparison* step.

10 A *cell geometry estimation* block provides an estimate γ_5 of the ratio between received intracell power and noise-plus-intercell interference power (or its inverse), or an estimate of the ratio between total received power and noise-plus-intercell interference power (or its inverse). An example of a cell geometry estimation technique that can be used is described in our copending application [PWF Ref.
15 316036GB]. Alternatively, any known technique for estimating signal to disturbance ratios on an incoming radio signal can be used, where disturbance is interference or noise or both. An example of signal to disturbance ratio estimation for a wireless cellular system is given in M. Turkboylari and G. L. Stuber, "An Efficient Algorithm for Estimating the Signal-to-Interference Ratio in TDMA Cellular
20 Systems", IEEE Transactions on Communications, vol. 46, no. 6, pp. 728-731, June 1998. As a further alternative, an estimate of the signal to disturbance ratio γ_6 of the estimated channel response can be used, or any other indication of the quality of the available channel estimate.

25 In addition to switching between the rake and equaliser, in the case that the equaliser 16 has been selected the channel parameters estimated by the channel parameter estimation function 10 can be used to select the parameters θ_n , $n = 1, \dots, N_E$ for the implementation of the equaliser 16.

30 Figure 5 is a schematic block diagram for the selection of a set of equaliser parameters within the equaliser parameter selection function 14.

The time window W for estimation of the channel impulse response in the equaliser can be selected on the basis of an estimate of the channel delay spread γ_3 (block 14a of Figure 5).

5 The memory of an appropriate filter for estimation of the channel impulse response (block 14b of Figure 5) and the frequency of update of the estimated channel impulse response (block 14c of Figure 5) can be selected on the basis of an estimate of the degree of channel non-stationarity or temporal selectivity, for example through an estimate of the channel Doppler spread γ_4 . The selection of
10 the channel estimation filter could also be based on an estimate γ_5 of the input signal-to-disturbance ratio or the cell geometry, and/or on an estimate γ_6 of the signal-to-disturbance ratio of the estimated channel response.

At intermediate to low signal to noise-plus-interference ratios, the total channel
15 estimation error can be reduced by setting to zero the estimated channel coefficients with amplitude lower than a suitable threshold. The value of this threshold can be selected based on an estimate γ_5 of the input signal-to-disturbance ratio or the cell geometry, and/or on an estimate γ_6 of the signal-to-disturbance ratio for the estimated channel coefficients (block 14d of Figure 5).

20 The memory of appropriate filters for estimation of the input noise variance σ^2 , for example in the case of MMSE equalisation, can be made adaptive in the presence on non-stationary input noise by measuring the degree of non-stationarity of the input disturbance γ_7 (for instance, the time interval over which the noise is
25 approximately constant) (block 14c of Figure 5). On a completely different basis, the filtering may depend on the periodicity with which it is convenient to collect observations on the input noise - this in turn may be motivated simply by the need to reduce the implementation complexity in specific operating conditions or under critical processing requirements.

30 The number of equaliser coefficients (i.e., the equaliser time span) can be selected for example on the basis of an estimate of the channel length or the channel delay

spread γ_3 and the position of the channel zeros in the z-plane γ_4 (block 14f of Figure 5).

5 The number of feedforward and feedback equaliser coefficients in the case of decision feedback equalisation can similarly be based on estimates of the channel out-of-window energy γ_2 and/or of the channel length (or the channel delay spread) γ_3 and the position of the channel zeros in the z-plane γ_4 (block 14g of Figure 5).

10 The frequency of update of the equaliser coefficients in the case of block equalisation, or the coefficient step size in the case of adaptive equalisation, can be selected on the basis of an estimate of the degree of channel non-stationarity or temporal selectivity, e.g. through an estimate of a channel Doppler spread γ_1 (block 14h of Figure 5).

15 The equaliser delay can be selected on the basis of an estimate of the channel phase characteristics derived from location of the channel zeros in the z-plane γ_4 (block 14i of Figure 5).

20 Reference will now be made to Figure 6 which is a schematic block diagram illustrating the selection of a particular equalisation algorithm based on the estimated channel conditions. While the sequence described below represents one useful embodiment of the invention, it will be appreciated that any other sequence can be utilised to implement selection of the appropriate equaliser
25 algorithm.

Level 6a in Figure 6 denotes the selection of a linear or non-linear equaliser structure. Linear equalisation based on a transversal filter structure has been employed since the early work of Lucky (R. W. Lucky, "Automatic Equalization for
30 Digital Communication", Bell System Technical Journal, vol. 44, pp. 547-588, April 1965), Proakis and Miller (J. G. Proakis and J. H. Miller, "An Adaptive receiver for Digital Signaling Through Channels with Intersymbol Interference", IEEE Transactions on Information Theory, vol. 15, no. 4, pp. 484-497, July 1969) and

others (see S. U. H. Qureshi "Adaptive Equalization", Proceedings of the IEEE, vol. 73, no. 9, pp. 1349-1387, September 1985 and references therein). Non-linear equalisers include decision-feedback equalisers (described for example in J. Salz, "Optimum Mean Square Decision Feedback Equalization", Bell System Technical Journal, vol. 52, pp. 1341-1373, October 1973, and C. A. Belfiore and J. H. Park, Jr., "Decision Feedback Equalization", Proceedings of the IEEE, vol. 67, no. 8, pp. 1143-1156, August 1979) and maximum-likelihood (ML) or maximum a posteriori probability (MAP) trellis equalisers (described for example in G. D. Forney, Jr., "Maximum Likelihood Sequence Estimation of Digital Sequences in the Presence of Intersymbol Interference", IEEE Transactions on Information Theory, vol. 18, no. 3, pp. 363-378, May 1972, and L. R. Bahl, J. Cocke, F. Jelinek, and Raviv, "Optimal Decoding of Linear Codes for Minimizing Symbol Error Rate", IEEE Transactions on Information Theory, vol. 20, pp. 284-287, March 1974). Linear and non-linear equalisers are also discussed in S. Benedetto, E. Biglieri, and V. Castellani, "Digital Transmission Theory", Englewood Cliffs, NJ, Prentice-Hall, 1987 and D. P. Taylor, G. M. Vitetta, B. D. Hart, and A. Mämmelä, "Wireless Channel Equalization", European Transactions on Telecommunications, vol. 9, no. 2, pp. 117-143, March 1998. A criterion for making the choice between a linear or non-linear equaliser can be based for example on the location of channel zeros in the z-plane γ_4 . In addition, this selection could depend on specific transmission conditions. For instance, in an HSDPA system, the use of a decision feedback equaliser (that is, having a non-linear structure) may be limited to a condition where the user is allocated a significant percentage of the downlink power – which determines the portion of the downlink signal that can be used for decision feedback without requiring to make decisions on other user's data.

Level 6b in Figure 6 denotes the selection of Baud-spaced or fractionally-spaced equaliser structure. Baud-spaced (symbol- or chip-spaced) and fractionally spaced equalisers are described for example in S. U. H. Qureshi "Adaptive Equalization", Proceedings of the IEEE, vol. 73, no. 9, pp. 1349-1387, September 1985 and J. R. Treichler, I. Fijalkow, and C. R. Johnson, Jr., "Fractionally Spaced Equalizers", IEEE Signal Processing Magazine, vol. 13, no. 3, pp. 65-81, May 1996. This selection is made based for instance on the location of the channel

zeros in the z-plane γ_4 , and could optionally take into account the amount of excess transmission bandwidth (roll-off factor of transmit and receive filters).

It will be clear that either baud-spaced or fractionally spaced design can be used
5 with either of the linear or non-linear selections.

Level 6c in Figure 6 denotes the selection of the equaliser cost function, specifically between the options of Minimum Mean-Square Error (MMSE) criterion, Least-Squares (LS) criterion, Zero-Forcing (ZF) criterion, or a criterion based on a
10 different cost, including the maximum-likelihood (ML) criterion and the maximum a posteriori probability (MAP) criterion. MMSE, LS, ZF and ML equalizers are described in S. U. H. Qureshi "Adaptive Equalization", Proceedings of the IEEE, vol. 73, no. 9, pp. 1349-1387, September 1985 and S. Benedetto, E. Biglieri, and V. Castellani, "Digital Transmission Theory", Englewood Cliffs, NJ, Prentice-Hall,
15 1987, while MAP equalisers are discussed in D. P. Taylor, G. M. Vitetta, B. D. Hart, and A. Mämmelä, "Wireless Channel Equalization", European Transactions on Telecommunications, vol. 9, no. 2, pp. 117-143, March 1998 and C. Luschi et al., "Advanced Signal Processing Algorithms for Energy-Efficient Wireless Communications", Proceedings of the IEEE vol. 88, no. 10, pp. 1633-1650, October
20 2000. Parameters that can be used to select between these criteria include an estimate of the signal-to-disturbance ratio or other parameters indicative of the statistical distribution of the disturbance. For instance, acceptable performance can be obtained for high signal-to-disturbance ratios using the ZF criterion. On the other hand, the use of a LS equaliser is preferable with respect to a MMSE
25 equaliser in the presence of non-Gaussian disturbance.

Level 6d in Figure 6 denotes the choice between equaliser block processing or the implementation of a tap adaptation rule. The selection between these two strategies may be made dependent on the degree of channel non-stationarity or
30 temporal selectivity, e.g. through an estimate of a channel Doppler spread γ_1 .

Block processing is mentioned for example in A. Klein, "Data Detection Algorithms Specially Designed for the Downlink of CDMA Mobile Radio Systems", in

Proceedings of IEEE Vehicular Technology Conference, vol. 1, Phoenix, AZ, May 1997, pp. 203-207. An adaptive algorithm is mentioned in K. Hooli, M. Latva-aho and M. Juntti, "Performance Evaluation of Adaptive Chip-Level Channel Equalizers in WCDMA Downlink", in Proceedings of IEEE International Conference on
5 Communications, vol. 6, Helsinki, Finland, June 2001, pp. 1974-1979.

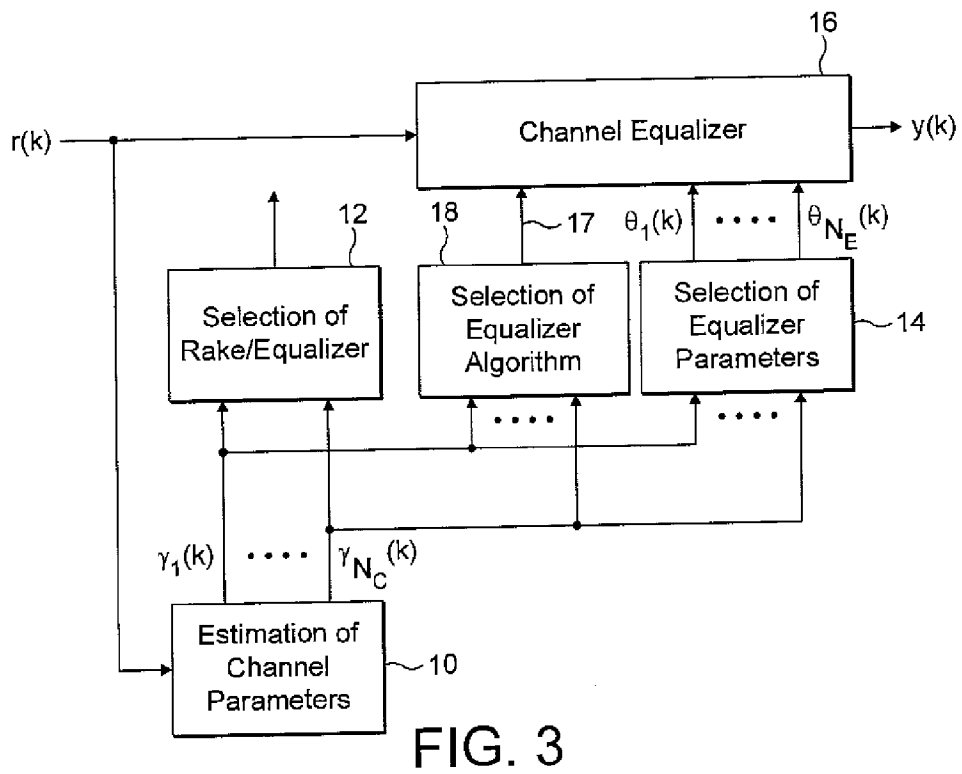
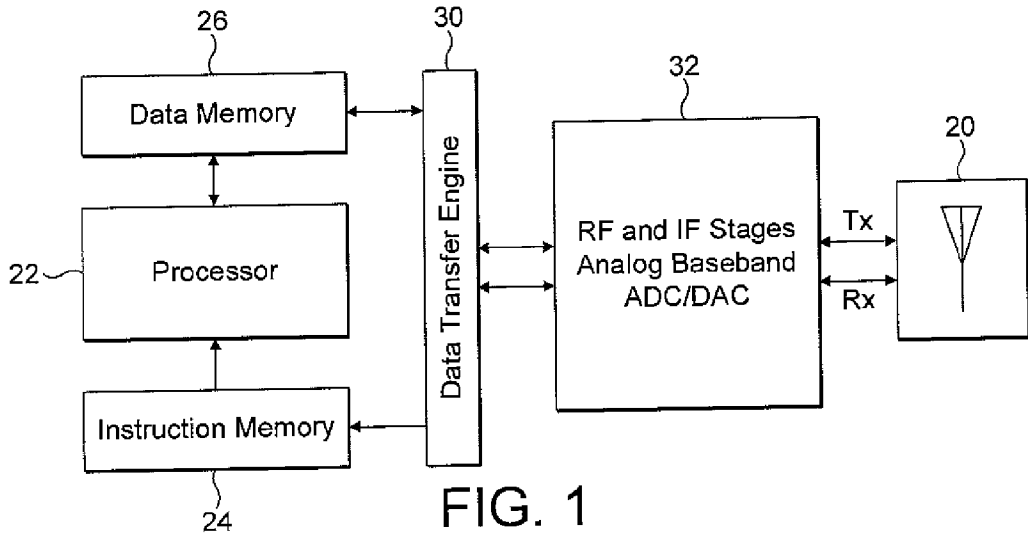
CLAIMS:

1. A radio receiver for a wireless communications system comprising:
channel equalisation means arranged to receive samples of an incoming
5 signal and to generate an equalised output, said channel equalisation means
comprising means for processing said digital samples in accordance with an
equaliser algorithm;
means for estimating parameters of a channel over which the incoming
signal has been transmitted; and
10 means for selecting from a plurality of equaliser algorithms an equaliser
algorithm for execution by the processing means based on at least one said
estimated channel parameter.
2. A receiver according to claim 1, comprising a memory coupled to said
15 processing means and holding said plurality of equaliser algorithms.
3. A receiver according to claim 1 or 2, wherein the plurality of algorithms
includes at least one linear and at least one non-linear structure.
- 20 4. A receiver according to claim 1 or 2, wherein the plurality of algorithms
includes at least one Baud-spaced and at least one fractionally-spaced structure.
5. A receiver according to claim 1 or 2, wherein the plurality of algorithms
includes algorithms with different equaliser cost functions.
25
6. A receiver according to claim 5, wherein the cost functions are based on at
least two among an MMSE criterion, a LS criterion, a ZF criterion, a ML criterion
or a MAP criterion.
- 30 7. A receiver according to claim 1, comprising means for selecting, from a set
of equaliser parameters and based on at least one said estimated channel
parameter, at least one of said equaliser parameters for use in the selected
equaliser algorithm,

8. A receiver according to claim 1, wherein the estimated channel parameters are selected from the group comprising:
- a parameter representing the degree of non-stationarity of the channel;
 - a parameter providing an estimate of channel length or channel delay spread;
 - a parameter representing location of channel zeros in the z plane;
 - a parameter representing signal-to-disturbance ratios of the estimated channel; and
 - a parameter representing the degree of non-stationarity of input disturbance on the channel.
9. A method of processing radio communication signals in a radio receiver, the method comprising:
- receiving digital samples of an incoming radio communication signal and processing those samples in accordance with an equaliser algorithm;
 - estimating at least one parameter of a channel over which the incoming signal has been transmitted; and
 - selecting said equaliser algorithm from a plurality of equaliser algorithms based on at least one said estimated channel parameter.
10. A method according to claim 9, wherein the step of selecting said equaliser algorithm comprises selecting between an equaliser algorithm with a linear structure and an equaliser algorithm with a non-linear structure.
11. A method according to claim 9, wherein the step of selecting said equaliser algorithm comprises selecting between a Baud-spaced structure and a fractionally-spaced structure.
12. A method according to claim 9, wherein the plurality of equaliser algorithms include algorithms with different equaliser cost functions, and the step of selecting said equaliser algorithm comprises selecting one of said different equaliser cost functions.

13. A method according to claim 12, wherein the cost functions are based on at least two among an MMSE criterion, a LS criterion, a ZF criterion, a ML criterion or a MAP criterion.
- 5 14. A method according to claim 10, wherein the step of selecting between a linear and a non-linear structure is based on a channel parameter representing the location of channel zeros in the z plane.
- 10 15. A method according to claim 10, wherein the step of selecting between a linear and a non-linear structure comprises determining a percentage of downlink power allocated to a user.
- 15 16. A method according to claim 11, wherein the step of selecting between a Baud-spaced and a fractionally-spaced structure is based on the channel parameter representing the location of channel zeros in the z plane.
- 20 17. A method according to claim 15 or 16, wherein the step of selecting between a Baud-spaced and a fractionally-spaced structure takes into account an amount of excess transmission bandwidth.
- 25 18. A method according to claim 12 or 13, wherein the step of selecting one of said equaliser cost functions is based on a parameter indicative of a signal to disturbance ratio.
- 30 19. A method according to claim 12 or 13, wherein the step of selecting one of said equaliser cost functions is based on a channel parameter indicative of statistical distribution of disturbance.
20. A method according to claim 9, wherein the plurality of algorithms include a block processing algorithm and a tap adaptation algorithm, wherein the step of selecting one of said algorithms is based on a channel parameter indicative of mobility of the channel.

21. A method according to claim 9, wherein the step of selecting said equaliser algorithm comprises:
- selecting between a linear and a non-linear structure;
 - selecting between a Baud-spaced and a fractionally-spaced structure; and
 - 5 selecting one of a plurality of different equaliser cost functions.
22. A method according to claim 21, further comprising the step of selecting between an equaliser block processing and a tap adaptation rule.



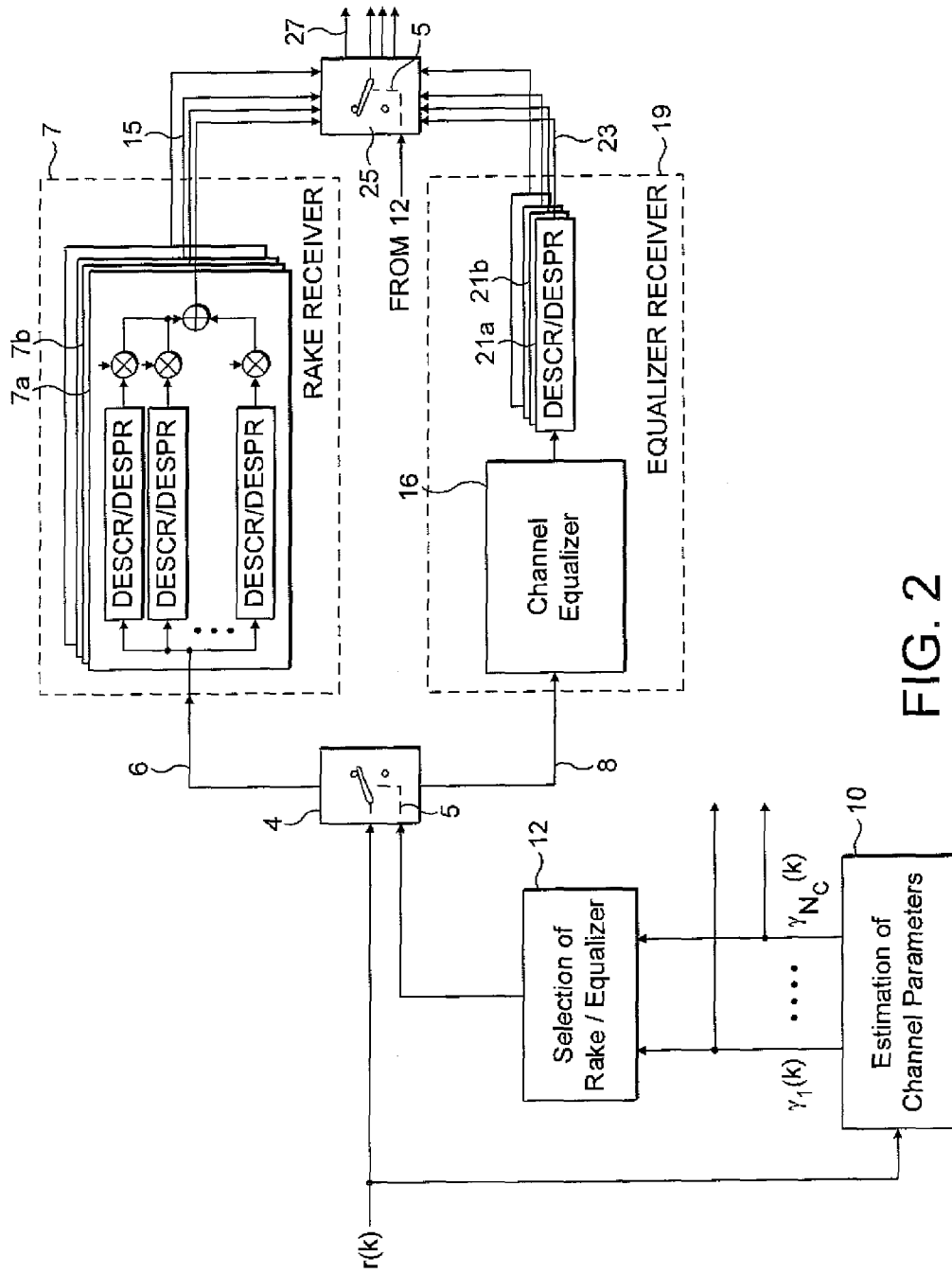


FIG. 2

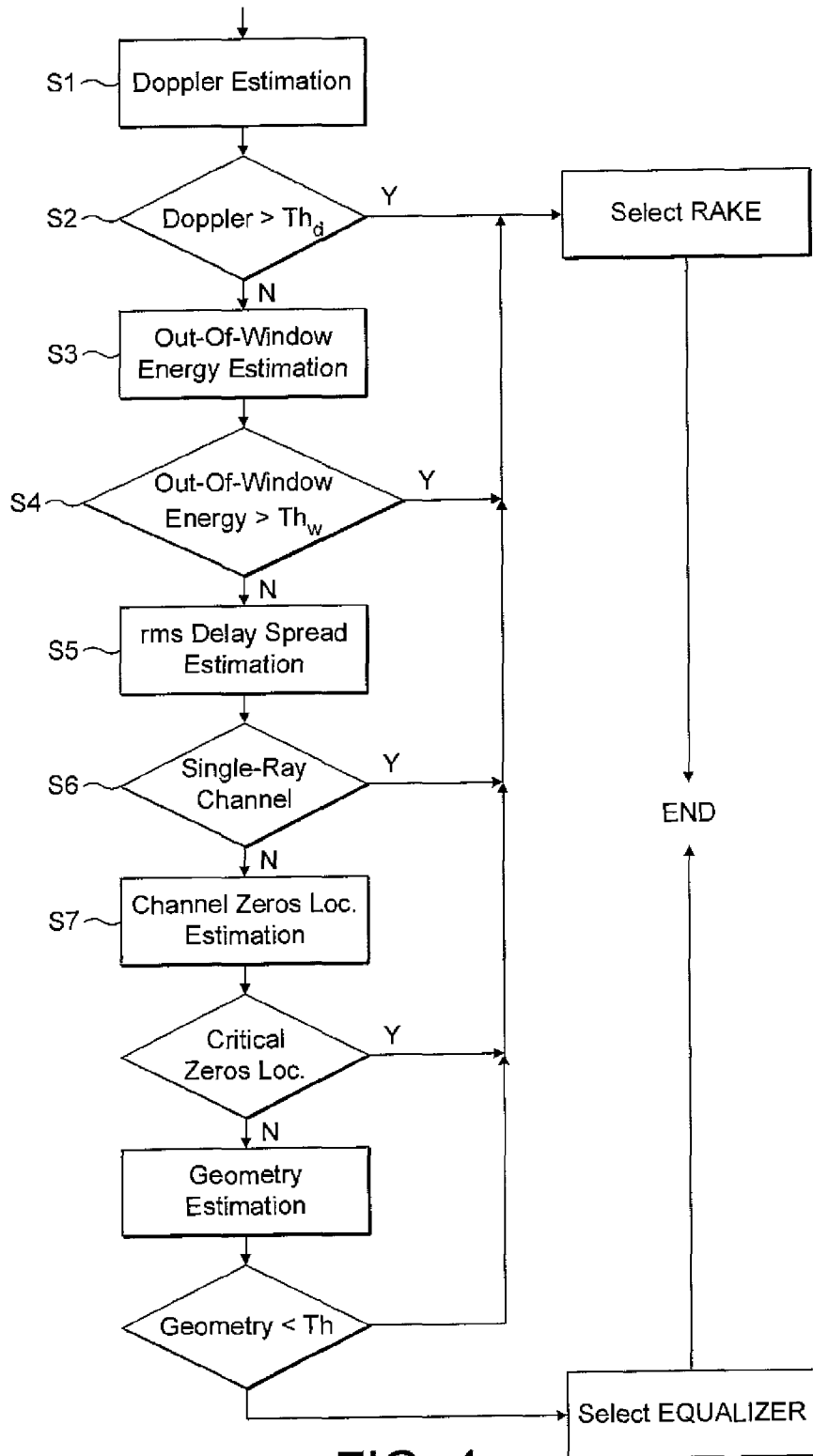


FIG. 4

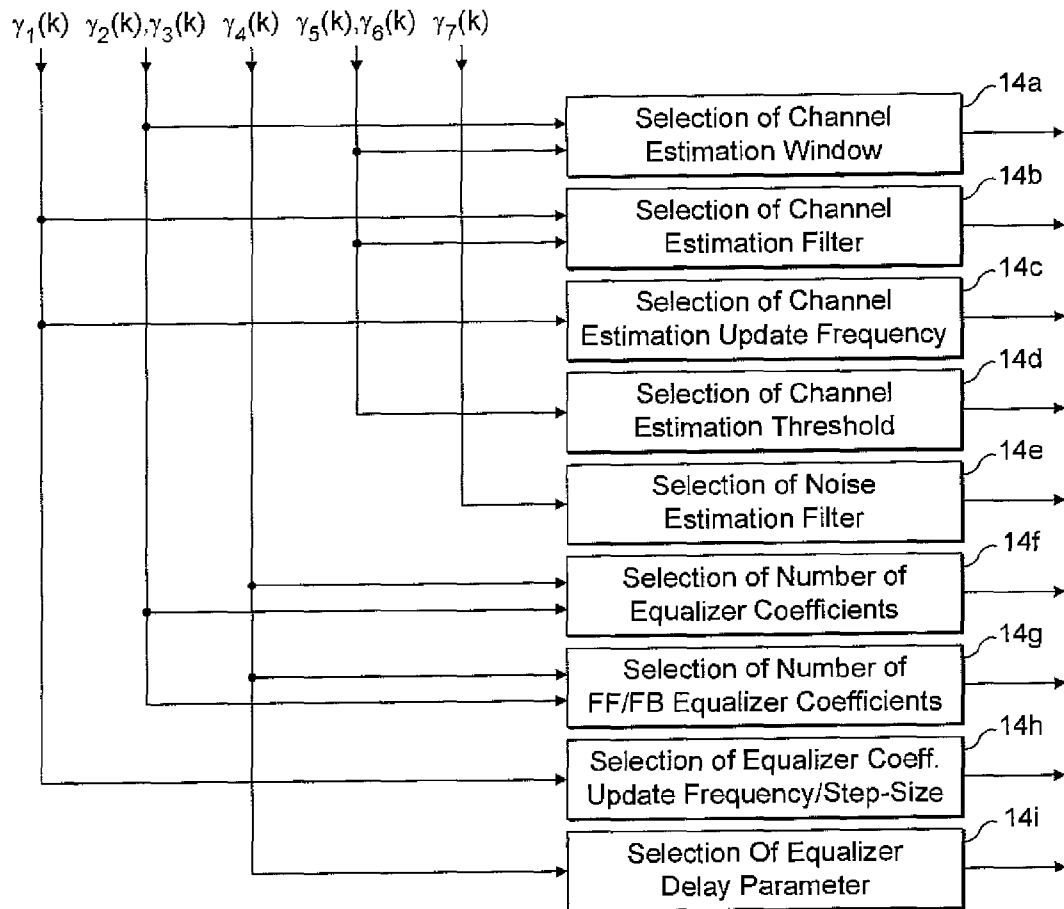


FIG. 5

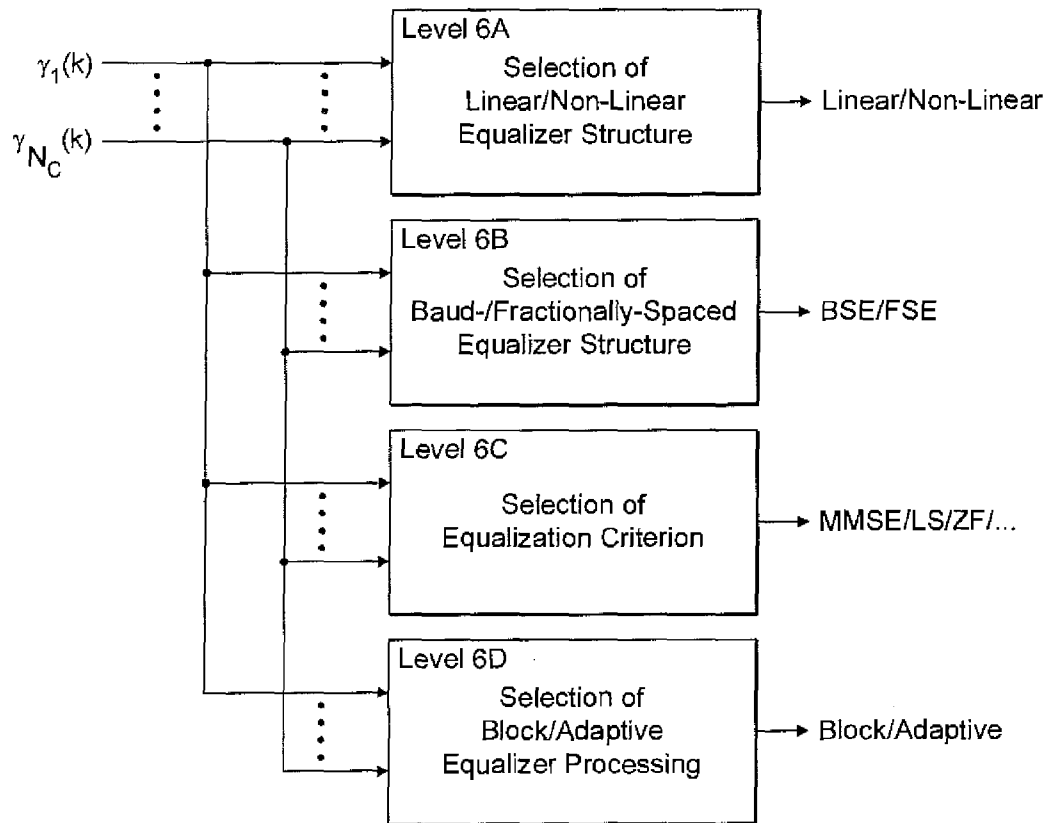


FIG. 6