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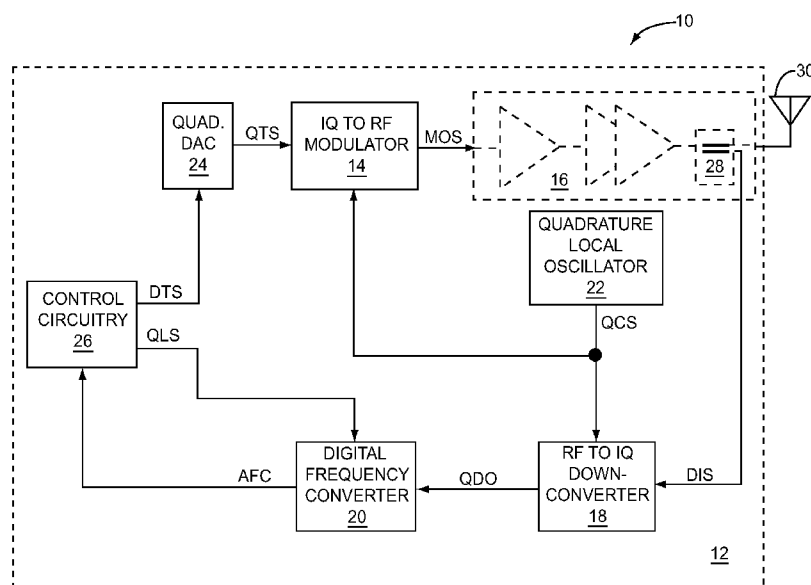


FIG. 1

(57) Abstract: A method and apparatus for measuring a complex gain of a transmit path are disclosed. During a test mode, an IQ to radio frequency modulator modulates a quadrature RF carrier signal using a quadrature test signal. An RF to IQ down-converter down-converts a down-converter RF input signal to provide a quadrature down-converter output signal using the quadrature RF carrier signal. The down-converter RF input signal is based on the quadrature test signal and the gain of the transmit path. A digital frequency converter frequency converts the quadrature down-converter output signal, providing an averaged frequency converter output signal, which is a quadrature direct current signal representative of an amplitude of the quadrature test signal and the gain of the transmit path. Therefore, a measured gain of the transmit path is based on the amplitude of the quadrature test signal and averaged frequency converter output signal.

RUGGED IQ RECEIVER BASED RF GAIN MEASUREMENTSPriority Claims

- 5 **[0001]** The present application claims priority to U.S. provisional patent application number 61/491,416, filed May 31, 2011. Further, U.S. provisional patent application number 61/491,416 is hereby incorporated herein by reference in its entirety.

Field of the Disclosure

- 10 **[0002]** Embodiments of the present disclosure relate to radio frequency (RF) transmitter circuitry, which may be used in RF communications systems, and calibration of the RF transmitter circuitry.

Background of the Disclosure

- 15 **[0003]** As wireless communications technologies evolve, wireless communications systems become increasingly sophisticated. As such, wireless communications protocols continue to expand and change to take advantage of the technological evolution, which may provide support for increasing numbers of simultaneous users in a given RF communications
20 space. In this regard, close management and control of RF transmitters utilized by the simultaneous users may be required, thereby requiring ongoing adjustments of the RF transmitters. RF gains of the RF transmitters may vary with different operational parameters, such as output power, power amplifier supply voltage, type of RF modulation, and the like. As such, certain RF
25 transmitter adjustments may be required based on RF gain. Such adjustments may include changes in transmitter pre-distortion, changes in envelope tracking system operation, changes in transmitter bias, and the like. Therefore, pre-determining a complex RF gain of a transmit path of a wireless device may be useful in making adjustments to the RF transmitter of the
30 wireless device. Thus, there is a need for a pre-determined complex RF gain in the transmit path of the wireless device.

Summary of the Embodiments

[0004] Embodiments of the present disclosure relate to a method and an apparatus for measuring a complex gain of a transmit path. Circuitry includes an IQ to RF modulator, an RF to IQ down-converter, and a digital frequency
5 converter. During a test mode, the IQ to RF modulator modulates a quadrature RF carrier signal using a quadrature test signal. During the test mode, the RF to IQ down-converter down-converts a down-converter RF input signal to provide a quadrature down-converter output signal using the quadrature RF carrier signal. The down-converter RF input signal is based on
10 the quadrature test signal and the complex gain of the transmit path. During the test mode, the digital frequency converter frequency converts the quadrature down-converter output signal to provide an averaged frequency converter output signal, which is a quadrature DC signal that is representative of an amplitude and phase of the quadrature test signal and the complex gain
15 of the transmit path. The quadrature down-converter output signal is synchronized to the quadrature test signal. A measured complex gain of the transmit path is based on the amplitude and phase of the quadrature test signal and the averaged frequency converter output signal.

[0005] The RF to IQ down-converter is part of an IQ receiver, which may
20 be relatively inexpensive. Such IQ receivers may have certain shortcomings, such as RF carrier leakage, interference from RF images, and the like, that adversely affect complex gain measurements. However, by incorporating the digital frequency converter into the IQ receiver and using a special test signal, as described, the effects of such shortcomings are significantly reduced,
25 thereby ruggedizing the IQ receiver when making complex gain measurements.

[0006] Those skilled in the art will appreciate the scope of the present disclosure and realize additional aspects thereof after reading the following detailed description of the preferred embodiments in association with the
30 accompanying drawing figures.

Brief Description of the Drawing Figures

[0007] The accompanying drawing figures incorporated in and forming a part of this specification illustrate several aspects of the disclosure, and together with the description serve to explain the principles of the disclosure.

5 **[0008]** Figure 1 shows an RF communications system during a test according to one embodiment of the RF communications system.

[0009] Figure 2 shows the RF communications system during the test mode according to an alternate embodiment of the RF communications system.

10 **[0010]** Figure 3 shows the RF communications system during the test mode according to an additional embodiment of the RF communications system.

[0011] Figure 4 shows the RF communications system during the normal operating mode according to another embodiment of the RF communications system.

15 **[0012]** Figure 5 illustrates a process for measuring a complex gain of a transmit path illustrated in Figure 1 according to one embodiment of the RF communications system.

[0013] Figure 6 shows the RF communications system during the test mode according to a further embodiment of the RF communications system.

[0014] Figure 7 shows details of an IQ to RF modulator illustrated in Figure 6 according to one embodiment of the IQ to RF modulator.

[0015] Figure 8 shows details of an RF to IQ down-converter illustrated in Figure 6 according to one embodiment of the RF to IQ down-converter.

25 **[0016]** Figure 9 shows details of a digital frequency converter illustrated in Figure 6 according to one embodiment of the digital frequency converter.

[0017] Figures 10A, 10B, 10C, and 10D are graphs illustrating an in-phase local oscillator signal, a quadrature-phase local oscillator signal, an in-phase down-converter output signal, and a quadrature-phase down-converter output signal, respectively, shown in Figure 9 according to one embodiment of the RF communications system.

30 **[0018]** Figures 11A, 11B, 11C, and 11D are graphs illustrating the in-phase local oscillator signal, the quadrature-phase local oscillator signal, the in-phase down-converter output signal, and the quadrature-phase down-

converter output signal, respectively, shown in Figure 9 according to an alternate embodiment of the RF communications system.

[0019] Figure 12 illustrates a process for processing an in-phase down-converter output signal and a quadrature-phase down-converter output signal
5 illustrated in Figure 9 according to one embodiment of the digital frequency converter.

[0020] Figure 13 illustrates a process for processing the in-phase down-converter output signal and the quadrature-phase down-converter output signal illustrated in Figure 9 according to an alternate embodiment of the
10 digital frequency converter.

Detailed Description of the Preferred Embodiments

[0021] The embodiments set forth below represent the necessary information to enable those skilled in the art to practice the disclosure and
15 illustrate the best mode of practicing the disclosure. Upon reading the following description in light of the accompanying drawing figures, those skilled in the art will understand the concepts of the disclosure and will recognize applications of these concepts not particularly addressed herein. It should be understood that these concepts and applications fall within the
20 scope of the disclosure and the accompanying claims.

[0022] Embodiments of the present disclosure relate to a method and an apparatus for measuring a complex gain of a transmit path. Circuitry includes an IQ to RF modulator, an RF to IQ down-converter, and a digital frequency converter. During a test mode, the IQ to RF modulator modulates a
25 quadrature RF carrier signal using a quadrature test signal. During the test mode, the RF to IQ down-converter down-converts a down-converter RF input signal to provide a quadrature down-converter output signal using the quadrature RF carrier signal. The down-converter RF input signal is based on the quadrature test signal and the complex gain of the transmit path. During
30 the test mode, the digital frequency converter frequency converts the quadrature down-converter output signal to provide an averaged frequency converter output signal, which is a quadrature DC signal that is representative of an amplitude and phase of the quadrature test signal and the complex gain of the transmit path. The quadrature down-converter output signal is

synchronized to the quadrature test signal. A measured complex gain of the transmit path is based on the amplitude and phase of the quadrature test signal and the averaged frequency converter output signal.

[0023] The RF to IQ down-converter is part of an IQ receiver, which may be relatively inexpensive. Such IQ receivers may have certain shortcomings, such as RF carrier leakage, interference from RF images, and the like, that adversely affect complex gain measurements. However, by incorporating the digital frequency converter into the IQ receiver and using a special test signal, as described, the effects of such shortcomings are significantly reduced, thereby ruggedizing the IQ receiver when making complex gain measurements.

[0024] Figure 1 shows an RF communications system 10 during a test mode according to one embodiment of the RF communications system 10. The RF communications system 10 includes antenna facing circuitry 12, which includes an IQ to RF modulator 14, a transmit path 16, an RF to IQ down-converter 18, a digital frequency converter 20, a quadrature local oscillator 22, a quadrature digital to analog converter (DAC) 24, and control circuitry 26. The transmit path 16 includes an RF coupler 28. The RF communications system 10 further includes an RF antenna 30. In one embodiment of the transmit path 16, the transmit path 16 is an uplink path. The transmit path 16 is coupled between the IQ to RF modulator 14 and the RF antenna 30. The transmit path 16 may further include portions of or all of one or more RF amplifier stages, RF switching circuitry, RF filter circuitry, one or more RF diplexers, one or more RF duplexers, other RF filtering, impedance matching circuitry, other RF front-end circuitry, the like, or any combination thereof coupled in series with the RF coupler 28. During the test mode, the RF communications system 10 functions to measure a complex gain of the transmit path 16.

[0025] The control circuitry 26 selects one of the test mode and a normal operating mode. As such, the antenna facing circuitry 12 operates in the selected one of the test mode and the normal operating mode. In one embodiment of the RF communications system 10, during the test mode, the control circuitry 26 provides a digital quadrature test signal DTS to the quadrature DAC 24, which converts the digital quadrature test signal DTS

from a digital signal into an analog signal. Further, the control circuitry 26 provides a quadrature local oscillator signal QLS to the digital frequency converter 20. The quadrature local oscillator signal QLS is a digital signal. Specifically, during the test mode, the quadrature DAC 24 receives and
5 digital-to-analog converts the digital quadrature test signal DTS to provide a quadrature test signal QTS, which is an analog signal, to the IQ to RF modulator 14.

[0026] During the test mode, the quadrature local oscillator 22 provides a quadrature RF carrier signal QCS to the IQ to RF modulator 14 and to the RF
10 to IQ down-converter 18. During the test mode, the IQ to RF modulator 14 modulates the quadrature RF carrier signal QCS using the quadrature test signal QTS to provide a RF modulator output signal MOS to the transmit path 16. During the test mode, the RF coupler 28 couples a portion of an RF signal flowing through the RF coupler 28 to provide a down-converter RF
15 input signal DIS to the RF to IQ down-converter 18. The RF signal flowing through the RF coupler 28 is based on the RF modulator output signal MOS. As such, the RF signal flowing through the RF coupler 28 is representative of the quadrature test signal QTS and the complex gain of the transmit path 16. In this regard, the portion of an RF signal flowing through the RF coupler 28
20 and the down-converter RF input signal DIS are also representative of the quadrature test signal QTS and the complex gain of the transmit path 16. Further, the down-converter RF input signal DIS is based on the quadrature test signal QTS and the complex gain of the transmit path 16.

[0027] During the test mode, the RF to IQ down-converter 18 down-
25 converts the down-converter RF input signal DIS to provide a quadrature down-converter output signal QDO using the quadrature RF carrier signal QCS. In this regard, the quadrature down-converter output signal QDO is representative of an amplitude and phase of the quadrature test signal QTS and the complex gain of the transmit path 16. During the test mode, the
30 digital frequency converter 20 frequency converts the quadrature down-converter output signal QDO to provide an averaged frequency converter output signal AFC to the control circuitry 26 using the quadrature local oscillator signal QLS. The quadrature down-converter output signal QDO is synchronized to the quadrature test signal QTS. As such, the averaged

frequency converter output signal AFC is a quadrature DC signal that is representative of an amplitude and phase of the quadrature test signal QTS and the complex gain of the transmit path 16. Specifically, a measured complex gain of the transmit path 16 is based on an amplitude and phase of the quadrature test signal QTS, which correlates to an amplitude and phase of the digital quadrature test signal DTS, and a magnitude and phase of the averaged frequency converter output signal AFC. Therefore, the control circuitry 26 may determine the measured complex gain of the transmit path 16 based on the quadrature local oscillator signal QLS and the averaged frequency converter output signal AFC.

[0028] Figure 2 shows the RF communications system 10 during the test mode according to an alternate embodiment of the RF communications system 10. The RF communications system 10 illustrated in Figure 2 is similar to the RF communications system 10 illustrated in Figure 1, except the RF communications system 10 illustrated in Figure 2 further includes baseband facing circuitry 32. The antenna facing circuitry 12 includes the IQ to RF modulator 14, the transmit path 16, the RF to IQ down-converter 18, and the quadrature local oscillator 22, whereas the baseband facing circuitry 32 includes the digital frequency converter 20, the quadrature DAC 24, and the control circuitry 26.

[0029] Other embodiments of the RF communications system 10 may have different allocations of the IQ to RF modulator 14, the transmit path 16, the RF to IQ down-converter 18, the digital frequency converter 20, the quadrature local oscillator 22, the quadrature DAC 24, and the control circuitry 26 between the antenna facing circuitry 12 and the baseband facing circuitry 32. In one embodiment of the antenna facing circuitry 12, an RF front-end module provides the antenna facing circuitry 12. The RF front-end module includes at least one integrated circuit (IC). In one embodiment of the baseband facing circuitry 32, a baseband controller provides the baseband facing circuitry 32. The baseband controller includes at least one IC. In an alternate embodiment of the baseband facing circuitry 32, transceiver circuitry provides the baseband facing circuitry 32. The transceiver circuitry includes at least one IC.

[0030] Figure 3 shows the RF communications system 10 during the test mode according to an additional embodiment of the RF communications system 10. The RF communications system 10 illustrated in Figure 3 is similar to the RF communications system 10 illustrated in Figure 1, except the
5 RF communications system 10 illustrated in Figure 3 further includes the baseband facing circuitry 32 and the antenna facing circuitry 12 further includes a digital multiplexer 34. The baseband facing circuitry 32 includes baseband facing control circuitry 36, which is coupled to the control circuitry 26 via a digital communications bus 38. As such, the control circuitry 26 and
10 the baseband facing control circuitry 36 can communicate with one another via the digital communications bus 38.

[0031] Both the antenna facing circuitry 12 and the baseband facing circuitry 32 operate in the selected one of the test mode and the normal operating mode. In one embodiment of the RF communications system 10,
15 the baseband facing control circuitry 36 selects the one of the test mode and the normal operating mode and indicates the mode selection using the digital communications bus 38. During the test mode, the control circuitry 26 provides the digital quadrature test signal DTS to the digital multiplexer 34. During the normal operating mode, the baseband facing control circuitry 36
20 provides a digital quadrature transmit signal DTX to the digital multiplexer 34.

[0032] The digital multiplexer 34 provides a digital multiplexer output signal DMX to the quadrature DAC 24 based on forwarding either the digital quadrature test signal DTS or the digital quadrature transmit signal DTX. Specifically, during the test mode, the digital multiplexer 34 forwards the
25 digital quadrature test signal DTS to provide the digital multiplexer output signal DMX. During the normal operating mode, the digital multiplexer 34 forwards the digital quadrature transmit signal DTX to provide the digital multiplexer output signal DMX. In an alternate embodiment of the RF communications system 10, during the normal operating mode, the baseband
30 facing control circuitry 36 provides the digital quadrature transmit signal DTX to the digital multiplexer 34 via the digital communications bus 38 and the control circuitry 26. During the test mode, since the digital multiplexer output signal DMX is based on the digital quadrature test signal DTS, the quadrature

DAC 24 receives and digital-to-analog converts the digital multiplexer output signal DMX to provide the quadrature test signal QTS.

[0033] Figure 4 shows the RF communications system 10 during the normal operating mode according to another embodiment of the RF communications system 10. The RF communications system 10 illustrated in Figure 4 is similar to the RF communications system 10, except during the normal operating mode, the baseband facing control circuitry 36 provides the digital quadrature transmit signal DTX to the digital multiplexer 34. During the normal operating mode, the digital multiplexer 34 forwards the digital quadrature transmit signal DTX to provide the digital multiplexer output signal DMX. The quadrature DAC 24 receives and digital-to-analog converts the digital multiplexer output signal DMX to provide a quadrature transmit signal QTX instead of the quadrature test signal QTS.

[0034] Processing of the quadrature transmit signal QTX by the IQ to RF modulator 14 and the transmit path 16 during the normal operating mode may be similar to processing of the quadrature test signal QTS during the test mode. However, processing of the quadrature transmit signal QTX may include processing and forwarding the quadrature transmit signal QTX to the RF antenna 30. In one embodiment of the antenna facing circuitry 12, during the normal operating mode, feedback is used to feed a processed portion of the digital quadrature transmit signal QTX to the control circuitry 26 via the RF to IQ down-converter 18 and the digital frequency converter 20. In an alternate embodiment of the antenna facing circuitry 12, during the normal operating mode, feedback is not used. As such, during the normal operating mode, the RF to IQ down-converter 18 and the digital frequency converter 20 are not used.

[0035] During the normal operating mode, the IQ to RF modulator 14 RF modulates the quadrature RF carrier signal QCS using the quadrature transmit signal QTX to provide the RF modulator output signal MOS to the transmit path 16. Further, in one embodiment of the antenna facing circuitry 12, during the normal operating mode, the RF modulator output signal MOS is processed and forwarded to the RF antenna 30 via the transmit path 16.

[0036] Figure 5 illustrates a process for measuring the complex gain of the transmit path 16 illustrated in Figure 1 according to one embodiment of the RF

communications system 10. In this regard, all signals and apparatus elements in the process are illustrated in Figure 1. The process begins by modulating the quadrature RF carrier signal QCS using the quadrature test signal QTS (Step A10). The process continues by down-converting the down-converter RF input signal DIS to provide the quadrature down-converter output signal QDO, such that the down-converter RF input signal DIS is based on the quadrature test signal QTS and the complex gain of the transmit path 16 (Step A12).

[0037] The process progresses by frequency converting the quadrature down-converter output signal QDO to provide the averaged frequency converter output signal AFC, which is a quadrature DC signal that is representative of the amplitude and phase of the quadrature test signal QTS and the complex gain of the transmit path 16, such that the quadrature down-converter output signal QDO is synchronized to the quadrature test signal QTS (Step A14). The process concludes by extracting the complex gain of the transmit path 16 based on the amplitude and phase of the quadrature test signal QTS and the magnitude and phase of the averaged frequency converter output signal AFC (Step A16).

[0038] Figure 6 shows the RF communications system 10 during the test mode according to a further embodiment of the RF communications system 10. The RF communications system 10 illustrated in Figure 6 is similar to the RF communications system 10 illustrated in Figure 1, except the RF communications system 10 illustrated in Figure 6 shows details of the control circuitry 26 and details of the digital quadrature test signal DTS, the quadrature test signal QTS, the quadrature RF carrier signal QCS, the quadrature down-converter output signal QDO, and the averaged frequency converter output signal AFC. The digital quadrature test signal DTS has a digital in-phase test signal DTI and a digital quadrature-phase test signal DTQ. The quadrature test signal QTS has an in-phase test signal TSI and a quadrature-phase test signal TSQ.

[0039] A continuous wave (CW) signal is defined as an un-modulated signal of constant amplitude and frequency. In a first embodiment of the RF communications system 10, during the test mode, the digital in-phase test signal DTI is a CW signal and the digital quadrature-phase test signal DTQ is

a CW signal, such that an amplitude of the digital quadrature-phase test signal DTQ is about equal to an amplitude of the digital in-phase test signal DTI. Further, the digital quadrature-phase test signal DTQ is phase-shifted from the digital in-phase test signal DTI by about 90 degrees. Therefore, both
5 the in-phase test signal TSI and the quadrature-phase test signal TSQ are CW signals, such that an amplitude of the quadrature-phase test signal TSQ is about equal to an amplitude of the in-phase test signal TSI. Further, the quadrature-phase test signal TSQ is phase-shifted from the in-phase test signal TSI by about 90 degrees.

10 **[0040]** The quadrature RF carrier signal QCS has an in-phase carrier signal CSI and a quadrature-phase carrier signal CSQ. In the first embodiment of the RF communications system 10, during the test mode, the in-phase carrier signal CSI and the quadrature-phase carrier signal CSQ are both CW signals, such that an amplitude of the quadrature-phase carrier
15 signal CSQ is about equal to an amplitude of the in-phase carrier signal CSI. Further, the quadrature-phase carrier signal CSQ is phase-shifted from the in-phase carrier signal CSI by about 90 degrees.

[0041] The control circuitry 26 includes a digital local oscillator 40, a digital up-converter 42, and a control circuitry subset 44. During the test mode, the
20 digital local oscillator 40 provides a quadrature local oscillator signal QLS to the digital frequency converter 20 and to the digital up-converter 42. The quadrature local oscillator signal QLS has an in-phase local oscillator signal LSI and a quadrature-phase local oscillator signal LSQ. In the first embodiment of the RF communications system 10, during the test mode, the
25 in-phase local oscillator signal LSI and the quadrature-phase local oscillator signal LSQ are both CW signals, such that an amplitude of the quadrature-phase local oscillator signal LSQ is about equal to an amplitude of the in-phase local oscillator signal LSI. Further, the quadrature-phase local oscillator signal LSQ is phase-shifted from the in-phase local oscillator signal
30 LSI by about 90 degrees.

[0042] During the test mode, the control circuitry subset 44 provides a digital test magnitude signal DTM to the digital up-converter 42. The digital up-converter 42 up-converts the digital test magnitude signal DTM using the quadrature local oscillator signal QLS to provide the digital quadrature test

signal DTS. In one embodiment of the digital up-converter 42, the digital up-converter 42 provides the digital in-phase test signal DTI based on the in-phase local oscillator signal LSI and provides the digital quadrature-phase test signal DTQ based on the quadrature-phase local oscillator signal LSQ, such that magnitudes of the digital in-phase test signal DTI and the digital quadrature-phase test signal DTQ are based on the digital test magnitude signal DTM. Further, a frequency of the digital in-phase test signal DTI is about equal to a frequency of the in-phase local oscillator signal LSI, and a frequency of the digital quadrature-phase test signal DTQ is about equal to a frequency of the quadrature-phase local oscillator signal LSQ.

[0043] In a first embodiment of the digital up-converter 42, the digital in-phase test signal DTI is phase-shifted from the in-phase local oscillator signal LSI by about 180 degrees, and the digital quadrature-phase test signal DTQ is phase-shifted from the quadrature-phase local oscillator signal LSQ by about 180 degrees. In a second embodiment of the digital up-converter 42, the digital in-phase test signal DTI is about phase-aligned with the in-phase local oscillator signal LSI, and the digital quadrature-phase test signal DTQ is about phase-aligned with the quadrature-phase local oscillator signal LSQ.

[0044] The quadrature down-converter output signal QDO has an in-phase down-converter output signal DOI and a quadrature-phase down-converter output signal DOQ. The averaged frequency converter output signal AFC has an in-phase frequency converter output signal FCI and a quadrature-phase frequency converter output signal FCQ. Further, the digital frequency converter 20 provides the averaged frequency converter output signal AFC to the control circuitry subset 44.

[0045] Figure 7 shows details of the IQ to RF modulator 14 illustrated in Figure 6 according to one embodiment of the IQ to RF modulator 14. The IQ to RF modulator 14 includes a first in-phase RF mixer 46, a first quadrature-phase RF mixer 48, and an RF combiner 50. During the test mode, the first in-phase RF mixer 46 RF modulates the in-phase carrier signal CSI using the in-phase test signal TSI by mixing the in-phase carrier signal CSI and the in-phase test signal TSI to provide an in-phase RF signal RFI. During the test mode, the first quadrature-phase RF mixer 48 RF modulates the quadrature-phase carrier signal CSQ using the quadrature-phase test signal TSQ by

mixing the quadrature-phase carrier signal CSQ and the quadrature-phase test signal TSQ to provide a quadrature-phase RF signal RFQ. During the test mode, the RF combiner 50 receives and combines the in-phase RF signal RFI and the quadrature-phase RF signal RFQ to provide the RF modulator output signal MOS.

[0046] Figure 8 shows details of the RF to IQ down-converter 18 illustrated in Figure 6 according to one embodiment of the RF to IQ down-converter 18. The RF to IQ down-converter 18 includes a second in-phase RF mixer 52, a second quadrature-phase RF mixer 54, and an RF splitter 56. During the test mode, the RF splitter 56 receives and splits the down-converter RF input signal DIS to provide an in-phase side RF signal RSI and a quadrature-phase side RF signal RSQ. During the test mode, the second in-phase RF mixer 52 down-converts the in-phase side RF signal RSI using the in-phase carrier signal CSI by mixing the in-phase side RF signal RSI and the in-phase carrier signal CSI to provide the in-phase down-converter output signal DOI. During the test mode, the second quadrature-phase RF mixer 54 down-converts the quadrature-phase side RF signal RSQ using the quadrature-phase carrier signal CSQ by mixing the quadrature-phase side RF signal RSQ and the quadrature-phase carrier signal CSQ to provide the quadrature-phase down-converter output signal DOQ.

[0047] Figure 9 shows details of the digital frequency converter 20 illustrated in Figure 6 according to one embodiment of the digital frequency converter 20. The digital frequency converter 20 includes a quadrature analog-to-digital converter (ADC) 58, a complex multiplier 60, and averaging circuitry 62. During the test mode, the quadrature ADC 58 receives and analog-to-digital converts the quadrature down-converter output signal QDO to provide a digital quadrature down-converter signal DDO. The quadrature down-converter output signal QDO has the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ. The digital quadrature down-converter signal DDO has a digital in-phase down-converter signal DDI and a digital quadrature-phase down-converter signal DDQ.

[0048] In this regard, the quadrature ADC 58 receives and analog-to-digital converts the in-phase down-converter output signal DOI to provide the digital

in-phase down-converter signal DDI. Further, the quadrature ADC 58 receives and analog-to-digital converts the quadrature-phase down-converter output signal DOQ to provide the digital quadrature-phase down-converter signal DDQ. To provide accurate analog-to-digital conversions, a one-bit
5 resolution of the quadrature ADC 58 needs to be small compared to an amplitude of the in-phase down-converter output signal DOI and to an amplitude of the quadrature-phase down-converter output signal DOQ.

[0049] During the test mode, the complex multiplier 60 receives and multiplies the digital quadrature down-converter signal DDO and the

10 quadrature local oscillator signal QLS to provide a quadrature complex multiplier output signal CMO, which has an in-phase complex multiplier output signal CMI and a quadrature-phase complex multiplier output signal CMQ. The multiplication of the digital quadrature down-converter signal DDO and the quadrature local oscillator signal QLS is a complex multiplication. Since
15 the digital quadrature test signal DTS is based on the quadrature local oscillator signal QLS, the multiplication of the digital quadrature down-converter signal DDO and the quadrature local oscillator signal QLS is synchronized to the digital quadrature test signal DTS. In this regard, during one embodiment of the complex multiplier 60, the complex multiplier 60
20 functions as a synchronous down-mixer of the quadrature test signal QTS (Figure 6), which has a frequency offset. Therefore, the complex multiplier 60 synchronizes the quadrature down-converter output signal QDO to the quadrature test signal QTS (Figure 6).

[0050] During the test mode, the averaging circuitry 62 receives and
25 averages the quadrature complex multiplier output signal CMO to provide the averaged frequency converter output signal AFC. Specifically, the averaging circuitry 62 receives and averages the in-phase complex multiplier output signal CMI to provide the in-phase frequency converter output signal FCI, and receives and averages the quadrature-phase complex multiplier output signal
30 CMQ to provide the quadrature-phase frequency converter output signal FCQ. By averaging the quadrature complex multiplier output signal CMO, negative effects of certain shortcomings of the RF to IQ down-converter 18 (Figure 6) may be reduced. Such shortcomings may include RF carrier leakage between the quadrature local oscillator 22 (Figure 6) and the RF to IQ down-

converter 18 (Figure 6), interference from RF images as a result of mixing, quadrature, mismatch in the RF to IQ down-converter 18 (Figure 6), the like, or any combination thereof.

[0051] In one embodiment of the averaging circuitry 62, to minimize error, during the test mode, the averaging circuitry 62 averages the quadrature complex multiplier output signal CMO for an integer number of samples in one period of the digital quadrature test signal DTS (Figure 6) and an integer number of periods of the digital quadrature test signal DTS (Figure 6). In an alternate embodiment of the averaging circuitry 62, to minimize error, during the test mode, the averaging circuitry 62 averages the quadrature complex multiplier output signal CMO for a long time period relative to one period of the digital quadrature test signal DTS (Figure 6).

[0052] An equation relating a magnitude of the averaged frequency converter output signal AFC to the complex gain of the transmit path 16 (Figure 6) is presented. AFCM is a complex magnitude of the averaged frequency converter output signal AFC, which is a complex signal. DTSA is an amplitude of the digital quadrature test signal DTS (Figure 6). GAIN is the measured complex gain of the transmit path 16 (Figure 6). SF is a complex scaling factor. EQ. 1 is an equation for AFCM as shown below.

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$$\text{EQ. 1: } \text{AFCM} = \text{GAIN} \times \text{DTSA} \times \text{SF}.$$

[0053] The complex scaling factor compensates for gains and losses in the signal path other than the complex gain of the transmit path 16 (Figure 6). For example, the coupling factor of the RF coupler 28 (Figure 6) would be included in the complex scaling factor. By re-arranging EQ. 1, EQ. 2 is an equation for measured complex gain of the transmit path 16 (Figure 6) as shown below.

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$$\text{EQ. 2: } \text{GAIN} = \text{AFCM} / (\text{DTSA} \times \text{SF}).$$

[0054] To preserve information, in one embodiment of the RF communications system 10 (Figure 6), a sampling rate of the quadrature ADC 58 is about equal to a sampling rate of the quadrature DAC 24 (Figure 6).

However, the complex multiplier 60 must perform a complex multiplication for each quadrature sample provided by the quadrature ADC 58.

[0055] Therefore, to reduce the computing load of the complex multiplier 60, in an alternate embodiment of the RF communications system 10 (Figure 6), the sampling rate of the quadrature ADC 58 is less than the sampling rate of the quadrature DAC 24 (Figure 6). In this regard, some information in the quadrature down-converter output signal QDO is discarded. However, by sampling the quadrature down-converter output signal QDO at specific times, much of the relevant information in the quadrature down-converter output signal QDO may be extracted.

[0056] There is a delay from the quadrature local oscillator signal QLS to correlating information in the quadrature down-converter output signal QDO. This delay is a processing delay and is a result of processing quadrature local oscillator signal QLS based signals through the digital up-converter 42 (Figure 6), the quadrature DAC 24 (Figure 6), the IQ to RF modulator 14 (Figure 6), the transmit path 16, and the RF to IQ down-converter 18 (Figure 6).

Therefore, when the sampling rate of the quadrature ADC 58 is less than the sampling rate of the quadrature DAC 24 (Figure 6), in one embodiment of the quadrature ADC 58, sampling by the quadrature ADC 58 is delayed to compensate for the processing delay in the RF communications system 10 (Figure 6). To maximize extraction of useful information from the quadrature down-converter output signal QDO, in one embodiment of the quadrature ADC 58, the quadrature down-converter output signal QDO is sampled at correlating amplitude peaks of the in-phase local oscillator signal LSI and the quadrature-phase local oscillator signal LSQ.

[0057] As such, in a first embodiment of the quadrature ADC 58, the quadrature down-converter output signal QDO is sampled four times per period of the quadrature test signal QTS (Figure 6). In a second embodiment of the quadrature ADC 58, the quadrature down-converter output signal QDO is sampled eight times per period of the quadrature test signal QTS (Figure 6). In a third embodiment of the quadrature ADC 58, the quadrature down-converter output signal QDO is sampled sixteen times per period of the quadrature test signal QTS (Figure 6). In a fourth embodiment of the quadrature ADC 58, the quadrature down-converter output signal QDO is

sampled thirty-two times per period of the quadrature test signal QTS (Figure 6).

[0058] Figures 10A, 10B, 10C, and 10D are graphs illustrating the in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the in-phase down-converter output signal DOI, and the quadrature-phase down-converter output signal DOQ, respectively, shown in Figure 9 according to one embodiment of the RF communications system 10 (Figure 6). Both the in-phase local oscillator signal LSI and the quadrature-phase local oscillator signal LSQ have a quadrature leg amplitude 64. The in-phase local oscillator signal LSI has a positive in-phase amplitude peak 66 and a negative in-phase amplitude peak 68. The quadrature-phase local oscillator signal LSQ has a positive quadrature-phase amplitude peak 70 and a negative quadrature-phase amplitude peak 72.

[0059] In the embodiment of the RF communications system 10 (Figure 6) illustrated in Figures 10A, 10B, 10C, and 10D, the quadrature-phase test signal TSQ (Figure 6) is phase-shifted from the in-phase test signal TSI (Figure 6) by about 90 degrees and the quadrature-phase local oscillator signal LSQ is phase-shifted from the in-phase local oscillator signal LSI by about 90 degrees. The in-phase local oscillator signal LSI is about phase-aligned with the in-phase test signal TSI (Figure 6). However, the quadrature-phase test signal TSQ (Figure 6) is phase-shifted from the quadrature local oscillator signal QLS by about 180 degrees. The digital up-converter 42 (Figure 6) provides the 180 degree phase-shift between the quadrature-phase test signal TSQ (Figure 6) and the quadrature local oscillator signal QLS.

[0060] As such, the quadrature-phase test signal TSQ and the quadrature local oscillator signal QLS have counter-rotating IQ vectors. The counter-rotating IQ vectors allow the complex multiplier 60 (Figure 9) to synchronously down-mix the quadrature local oscillator signal QLS (Figure 9) and the quadrature test signal embedded in the quadrature down-converter output signal QDO (Figure 9) to extract the complex gain of the transmit path 16 (Figure 6) regardless of phase-alignment of the quadrature test signal and the quadrature local oscillator signal QLS (Figure 6). Therefore, the processing delay that was previously discussed does not affect the synchronous down-mixing. However, alternative embodiments of the RF communications system

10 (Figure 6) that do not incorporate counter-rotating IQ vectors may need to compensate for the effects of processing delay.

[0061] The in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ both illustrate
5 information that correlates with the in-phase local oscillator signal LSI and the quadrature-phase local oscillator signal LSQ, respectively. The correlating information in the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ is delayed from the in-phase local oscillator signal LSI and the quadrature-phase local oscillator
10 signal LSQ due to the processing delay. As a result, in embodiments of the RF communications system 10 (Figure 6) that do not incorporate counter-rotating IQ vectors, sampling by the quadrature ADC 58 may need to be delayed by a sample delay 74 to align the correlating information in the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ with the in-phase local oscillator signal LSI and the quadrature-phase local oscillator signal LSQ, respectively.

[0062] The in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ have a sample period 76, which is about equal to a period of the quadrature local oscillator signal QLS. The in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ are sampled four times per sample period 76. A first sample 78 of the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ is taken when the in-phase down-converter output signal DOI correlates to the positive in-phase
20 amplitude peak 66. A second sample 80 of the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ is taken when the quadrature-phase down-converter output signal DOQ correlates to the positive quadrature-phase amplitude peak 70. A third sample 82 of the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ is taken when the in-phase down-converter output signal DOI correlates to the negative in-phase
25 amplitude peak 68. A fourth sample 84 of the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ is

taken when the quadrature-phase down-converter output signal DOQ correlates to the negative quadrature-phase amplitude peak 72.

[0063] The first sample 78 of the in-phase down-converter output signal DOI has a first sample in-phase magnitude 86. The first sample 78 of the quadrature-phase down-converter output signal DOQ has a first sample quadrature-phase magnitude 88. The second sample 80 of the in-phase down-converter output signal DOI has a second sample in-phase magnitude 90. The second sample 80 of the quadrature-phase down-converter output signal DOQ has a second sample quadrature-phase magnitude 92. The third sample 82 of the in-phase down-converter output signal DOI has a third sample in-phase magnitude 94. The third sample 82 of the quadrature-phase down-converter output signal DOQ has a third sample quadrature-phase magnitude 96. The fourth sample 84 of the in-phase down-converter output signal DOI has a fourth sample in-phase magnitude 98. The fourth sample 84 of the quadrature-phase down-converter output signal DOQ has a fourth sample quadrature-phase magnitude 100.

[0064] To simplify the complex multiplier 60 (Figure 9), the quadrature leg amplitude 64 (Figure 10A) is scaled to be 1. In one embodiment of the RF communications system 10 (Figure 6), to simplify the complex multiplier 60 (Figure 9), during multiplication of the digital quadrature down-converter signal DDO (Figure 9) and the quadrature local oscillator signal QLS (Figure 9), a magnitude of the in-phase local oscillator signal LSI is 1, 0, or -1 and a magnitude of the quadrature-phase local oscillator signal LSQ is 1, 0, or -1.

[0065] Returning to Figure 9, the complex multiplier 60 performs a complex multiplication of the quadrature local oscillator signal QLS times the digital quadrature down-converter signal DDO to provide the quadrature complex multiplier output signal CMO. As such, in one embodiment of the RF communications system 10 (Figure 6), the quadrature local oscillator signal QLS may be represented as $LSI + jLSQ$, the digital quadrature down-converter signal DDO may be represented as $DDI + jDDQ$, and the quadrature complex multiplier output signal CMO may be represented as $CMI + jCMQ$. Further, the first sample in-phase magnitude 86 is represented as "86". The first sample quadrature-phase magnitude 88 is represented as "88". The second sample in-phase magnitude 90 is represented as "90". The

second sample quadrature-phase magnitude 92 is represented as "92". The third sample in-phase magnitude 94 is represented as "94". The third sample quadrature-phase magnitude 96 is represented as "96". The fourth sample in-phase magnitude 98 is represented as "98". The fourth sample quadrature-phase magnitude 100 is represented as "100".

[0066] In this regard, the table below shows magnitudes of the in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the digital in-phase down-converter signal DDI, the digital quadrature-phase down-converter signal DDQ, the in-phase complex multiplier output signal CMI, and the quadrature-phase complex multiplier output signal CMQ during the four samples previously described. To simplify calculations, the quadrature leg amplitude 64 (Figure 10A) is scaled to be 1.

SAMPLE	LSI	LSQ	DDI	DDQ	CMI	CMQ
FIRST	1	0	"86"	"88"	"86"	"88"
SECOND	0	-1	"90"	"92"	"-92"	"90"
THIRD	-1	0	"94"	"96"	"-94"	"-96"
FOURTH	0	1	"98"	"100"	"100"	"-98"

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[0067] From the table, the in-phase complex multiplier output signal CMI and the quadrature-phase complex multiplier output signal CMQ are easily provided by the complex multiplier 60. In one embodiment of the complex multiplier 60, for the first sample, the complex multiplier 60 need only forward the digital in-phase down-converter signal DDI to provide the in-phase complex multiplier output signal CMI and forward the digital quadrature-phase down-converter signal DDQ to provide the quadrature-phase complex multiplier output signal CMQ.

[0068] For the second sample, the complex multiplier 60 need only negate and forward the digital quadrature-phase down-converter signal DDQ to provide the in-phase complex multiplier output signal CMI, and forward the digital in-phase down-converter signal DDI to provide the quadrature-phase complex multiplier output signal CMQ. For the third sample, the complex

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multiplier 60 need only negate and forward the digital in-phase down-converter signal DDI to provide the in-phase complex multiplier output signal CMI, and negate and forward the digital quadrature-phase down-converter signal DDQ to provide the quadrature-phase complex multiplier output signal CMQ. For the fourth sample, the complex multiplier 60 need only negate and forward the digital in-phase down-converter signal DDI to provide the quadrature-phase complex multiplier output signal CMQ, and forward the digital quadrature-phase down-converter signal DDQ to provide the in-phase complex multiplier output signal CMI.

- 10 **[0069]** Figures 11A, 11B, 11C, and 11D are graphs illustrating the in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the in-phase down-converter output signal DOI, and the quadrature-phase down-converter output signal DOQ, respectively, shown in Figure 9 according to an alternate embodiment of the RF communications system 10 (Figure 6).
- 15 The in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the in-phase down-converter output signal DOI, and the quadrature-phase down-converter output signal DOQ illustrated in Figures 11A, 11B, 11C, and 11D are similar to the in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the in-phase down-converter output signal DOI, and the quadrature-phase down-converter output signal DOQ illustrated in Figures 10A, 10B, 10C, and 10D, except the in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the in-phase down-converter output signal DOI, and the quadrature-phase down-converter output signal DOQ illustrated in Figures 10A, 10B, 10C, and 10D are sinusoidal signals, whereas the in-phase local oscillator signal LSI, the quadrature-phase local oscillator signal LSQ, the in-phase down-converter output signal DOI, and the quadrature-phase down-converter output signal DOQ illustrated in Figures 11A, 11B, 11C, and 11D are square-wave signals.
- 20
- 25
- 30 **[0070]** As such, the in-phase test signal TSI (Figure 6) is approximately a square wave and the quadrature-phase test signal TSQ (Figure 6) is approximately a square wave. In one embodiment of the RF communications system 10 (Figure 6) sampling by the quadrature ADC 58 (Figure 9) is delayed by the sample delay 74 to allow a steady-state to be reached before sampling the quadrature down-converter output signal QDO (Figure 9). In this

regard, after each transition of the phase test signal TSI (Figure 6) is and the quadrature-phase test signal TSQ (Figure 6), multiplication of the digital quadrature down-converter signal DDO (Figure 9) and the quadrature local oscillator signal QLS (Figure 9) occurs after a steady-state of the digital quadrature down-converter signal DDO (Figure 9) is reached.

[0071] In one embodiment of the complex multiplier 60 (Figure 9), if the averaging circuitry 62 (Figure 9) is not capable of accepting negative values, the complex multiplier 60 (Figure 9) could add the four samples together to provide a sum to the averaging circuitry 62 (Figure 9). In this regard, the complex multiplier 60 (Figure 9) may be fairly simple. In one embodiment of the complex multiplier 60 (Figure 9), the complex multiplier 60 (Figure 9) is implemented in software running on a processor, such as a micro-controller. In an alternate embodiment of the complex multiplier 60 (Figure 9), the complex multiplier 60 includes multiplexers, digital summing circuitry (Figure 9), digital difference circuitry, and the like.

[0072] Figure 12 illustrates a process for processing the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ illustrated in Figure 9 according to one embodiment of the digital frequency converter 20 (Figure 9). This process may be part of the frequency converting the quadrature down-converter output signal QDO to provide the averaged frequency converter output signal AFC (Step A14) illustrated in Figure 5. The process describes adding the four samples together to provide a sum to the averaging circuitry 62 (Figure 9).

[0073] The process begins by providing and clearing an in-phase register (not shown) and a quadrature-phase register (not shown)(Step B10). The in-phase register (not shown) and the quadrature-phase register (not shown) are part of the complex multiplier 60 (Figure 9). The process continues by sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9) using the quadrature ADC 58 (Figure 9) to obtain a first in-phase sample and a first quadrature-phase sample, respectively (Step B12). The process progresses by adding the first in-phase sample to the in-phase register and adding the first quadrature-phase sample to the quadrature-phase register (Step B14).

[0074] The process continues by sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9) using the quadrature ADC 58 (Figure 9) to obtain a second in-phase sample and a second quadrature-phase sample,

- 5 respectively (Step B16). The process progresses by adding the second in-phase sample to the quadrature-phase register and subtracting the second quadrature-phase sample from the in-phase register (Step B18).

- [0075]** The process continues by sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9) using the quadrature ADC 58 (Figure 9) to obtain a third in-phase sample and a third quadrature-phase sample, respectively (Step B20). The process progresses by subtracting the third in-phase sample from the in-phase register and subtracting the third quadrature-phase sample from the quadrature-phase register (Step B22).

- 15 **[0076]** The process continues by sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9) using the quadrature ADC 58 (Figure 9) to obtain a fourth in-phase sample and a fourth quadrature-phase sample, respectively (Step B24). The process progresses by subtracting the fourth in-phase sample from the quadrature-phase register and adding the fourth quadrature-phase sample to the in-phase register (Step B26).

- [0077]** The process concludes by forwarding contents of the in-phase register and the quadrature-phase register to the averaging circuitry 62 (Figure 9) via the in-phase complex multiplier output signal CMI (Figure 9) and the quadrature-phase complex multiplier output signal CMQ (Figure 9), respectively (Step B28).

- [0078]** As previously mentioned, in one embodiment of the RF communications system 10 (Figure 6), the quadrature test signal QTS (Figure 6) is based on the quadrature local oscillator signal QLS (Figure 6) and there is a processing delay from the quadrature local oscillator signal QLS (Figure 9) to correlating information in the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9). Therefore, in one embodiment of the quadrature ADC 58 (Figure 9), sampling by the quadrature ADC 58 (Figure 9) is delayed to compensate

for the processing delay in the RF communications system 10 (Figure 6). In this regard, sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9) is delayed to compensate for the processing delay from the quadrature local oscillator signal QLS (Figure 9) to correlating information in the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9).

[0079] Figure 13 illustrates a process for processing the in-phase down-converter output signal DOI and the quadrature-phase down-converter output signal DOQ illustrated in Figure 9 according to an alternate embodiment of the digital frequency converter 20 (Figure 9). This process may be part of the frequency converting the quadrature down-converter output signal QDO to provide the averaged frequency converter output signal AFC (Step A14) illustrated in Figure 5. This process describes adding multiple samples together to provide a sum to the averaging circuitry 62 (Figure 9). In this regard, this process illustrated in Figure 13 is a generalized version of the process illustrated in Figure 12.

[0080] The process begins by providing and clearing an in-phase register (not shown) and a quadrature-phase register (not shown) (Step C10). The in-phase register (not shown) and the quadrature-phase register (not shown) are part of the complex multiplier 60 (Figure 9). The process continues by sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9) using the quadrature ADC 58 (Figure 9) to obtain an in-phase sample and a quadrature-phase sample, respectively (Step C12). The process progresses by adding or subtracting the in-phase sample to or from, respectively, one of the in-phase register and the quadrature-phase register (Step C14). The process continues by adding or subtracting the quadrature-phase sample to or from, respectively, another of the in-phase register and the quadrature-phase register (Step C16). The process proceeds by repeating the sampling the in-phase down-converter output signal DOI (Figure 9) and the quadrature-phase down-converter output signal DOQ (Figure 9), the adding or subtracting the in-phase sample, and the adding or subtracting the quadrature-phase sample, as necessary (Step C18). The process concludes by forwarding contents of

the in-phase register and the quadrature-phase register to the averaging circuitry 62 (Figure 9) via the in-phase complex multiplier output signal CMI (Figure 9) and the quadrature-phase complex multiplier output signal CMQ (Figure 9), respectively (Step C20).

- 5 **[0081]** Those skilled in the art will recognize improvements and modifications to the preferred embodiments of the present disclosure. All such improvements and modifications are considered within the scope of the concepts disclosed herein and the claims that follow. Appendix 1 includes information provided in U.S. provisional patent application number
- 10 61/491,416, filed May 31, 2011. This information is provided to support and clarify the invention.

APPENDIX 1**IMPAIRMENT RESISTANT CALIBRATION TECHNIQUE USING IQ
RECEIVER**

5

Background

[0082] In many systems like RF transmitters there is the need to calibrate and control either gain and/or phase of the system (like in envelope following or predistortion systems) or the output power of the system with enough accuracy, without having to build complex and current consuming feedback systems. In recent years, in the cellular and other industries, such feedback systems have begun to use low cost / low performance IQ receivers. Such choice has many advantages among which linearity and possibility to measure phase, but it also has many types of impairments that degrade the accuracy of measurement to the point of being barely usable in case high measurement accuracy is required. This is the case for example of Pseudo Envelope Following systems where transmitter feedback system can be used at production time to provide a very fast way to factory calibration of PA isoGain Vcc(Pin) rule.

Summary

[0083] The present disclosure relates to a simple method of using such feedback systems so that is insensitive to most of classical IQ receiver impairments, simple enough that it is possible to implement it directly on transceiver silicon or firmware without having to implement exotic hardware or software functions. The measurement method is designed to be used with IQ receiver like measurement systems, which is insensitive to most of the impairments common to such arrangements. Doing so can help improving significantly measurement accuracy without complexity overhead. This technique can be used wherever power or gain measurements are required, like cellular transmitters, envelope following systems, and the like. This may enable accurate power/gain calibration from low cost/low performance IQ receiver feedback path hardware.

[0084] Those skilled in the art will appreciate the scope of the present disclosure and realize additional aspects thereof after reading the following detailed description in association with the accompanying drawings.

5 Detailed Description

[0085] An example of a transmitter system using an IQ receiver as a feedback path is given in Figure 1. The local oscillator is shared between transmit and feedback path, such that feedback output will always be phase synchronous to transmit path.

10 **[0086]** Simple IQ receivers are using IQ demodulators. Such architecture usually has some well-known impairments that can degrade measurement accuracy if not properly managed. Those impairments are represented in Figure 2.

[0087] One method that may be used for calibration would be to use a test signal at local oscillator frequency (i.e. in the case of an IQ transmitter constant DC values for both I and Q). This obviously is not the best thing to do to be insensitive to feedback IQ receiver, as both DC “test signal”, DC resulting of carrier leakage and image (also at DC frequency) will be measured at receiver output, with no way to distinguish test signals from
15
20 impairments. Moreover, depending on (unpredictable) phase shift in the system, those different DC component with combine from out phase to in phase, resulting in some error that may be repeatable for a given unit in some given conditions, but that will be random unit to unit, condition to condition.

[0088] Another way to manage better with receiver impairments is to use
25 “AC” IQ signals like cosine and sine I and Qs, that is a CW RF test signal at a frequency different from carrier frequency. Doing so, it is now possible to distinguish the different components of output signal (see Figure 4).

DC can be estimated then removed from measured signal using a first measurement with no RF, then image can be managed averaging a few IQ
30 power or magnitude measurements as presence of image produces a slight amplitude modulation depending on image and wanted signal relative phase.

Assuming DC component was removed as described above:

$$Out(t) = Sig \cdot e^{j\omega t} + Img \cdot e^{-j(\omega t + \Phi)}$$

$$Out(t) = Sig \cdot [\cos(\varpi \cdot t) + j \cdot \sin(\varpi \cdot t)] + Img \cdot [\cos(\varpi \cdot t + \Phi) - j \cdot \sin(\varpi \cdot t + \Phi)]$$

$$P_{out}(t) = \frac{|Out(t)|^2}{R}$$

$$P_{out}(t) = \frac{[Sig \cdot \cos(\varpi \cdot t) + Img \cdot \cos(\varpi \cdot t + \Phi)]^2 + [Sig \cdot \sin(\varpi \cdot t) - Img \cdot \sin(\varpi \cdot t + \Phi)]^2}{R}$$

$$P_{out}(t) = \frac{Sig^2 + Img^2 + 2 \cdot Sig \cdot Img \cdot (\cos(\varpi \cdot t) \cdot \cos(\varpi \cdot t + \Phi) - \sin(\varpi \cdot t) \cdot \sin(\varpi \cdot t + \Phi))}{R}$$

5

$$P_{out}(t) = \frac{Sig^2 + Img^2 + 2 \cdot Sig \cdot Img \cdot \cos(2 \cdot \varpi \cdot t + \Phi)}{R}$$

Assuming cosine average is null across chosen averaging period of time (which means integration time much longer than test signal period or integer number of equally spaced samples during 1/2 test signal period):

$$10 \quad P_{Out_Avg} = \frac{Sig^2 + Img^2}{R}$$

Because Image power is usually significantly lower than wanted component of the output signal, average output power is usually a good estimation of actual signal power.

[0089] Two limitations of this method:

- 15
- DC is removed from signal prior to average power computation.
This means that DC estimate and DC drift of receiver during measurements needs to be good enough so that residual contribution can be neglected. This may be a correct assumption when calibrating a signal close to full receiver scale, but this may be incorrect for very
- 20
- low powers (like when calibrating low dynamic end of Pseudo Envelope Following, ET or pre-distortion systems).
 - Not possible to get phase information using this technique (pre-distortion systems).

[0090] Since that when using "AC" like I and Q test signals, all frequency

25 components are separated from each other, a better way to deal with

feedback receiver impairments would be to deal with bandwidth limited measurements around frequency of interest, that is test tone frequency offset.

[0091] However, since building a band pass measurement system centered on tone frequency would be too complex and cost ineffective, it may be easier to down convert digitally the feedback receiver output signal using a digital local oscillator at the exact test tone frequency offset opposite. This is similar operation as “synchronous demodulators” and translates back test tone frequency to DC, which is easier to process (a simple average can then reduce bandwidth and remove image and DC contributions). (See Figure 5.)

10

$$Out(t) = DC + Sig \cdot e^{j\omega t} + Img \cdot e^{-j(\omega t + \Phi)} + Noise(t)$$

Sig, *Img*, *DC* and *Noise(t)* are actually complex values.

After down conversion to “BaseBand”:

$$BB(t) = DC \cdot e^{-j\omega t} + Sig + Img \cdot e^{-j(2\omega t + \Phi)} + Noise(t) \cdot e^{-j\omega t}$$

15 With sufficient time averaging of this signal (either long enough averaging or integer number of samples in one test tone period), we should get:

$$BB_{Avg} = Sig + Noise_{Avg_contrib}$$

Contribution of everything except test tone and partly noise is cancelled.

[0092] Average test tone power is then easily calculated. Because this method uses voltage averaging, average result is then a complex number. It is therefore also possible to get phase information from this which is useful information for example to calibrate a pre-distortion system.

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[0093] Despite the attractiveness of “Synchronous Downmixing” technique presented above, this method is still rather complex to implement because of the presence of the digital oscillator and complex down mixer. For that reason it may still not be well adapted to a low cost implementation either directly on silicon or in the firmware of some transmitter/transceiver chipset.

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[0094] In such a case, using some specific cases of test signals and complex multiplication properties, it is still possible to implement this technique using a very low level of complexity.

[0095] The complexity of previously presented method lies at three places:

- 5 • Generation of test tones: may be implemented using DDS using sine/cosine tables.
- Digital down-mixer local oscillator: same as above.
- Digital down-mixer: complex multiplication is required here.

This can be simplified considering special case where sine/cosine have

10 simple expression (like $0, k \cdot \pi/4, k \cdot \pi/2, k \cdot \pi, \dots$).

Let's consider the following cases:

$$\begin{aligned}
 \text{Phase} &= \begin{bmatrix} \frac{\pi}{4} & \frac{3\pi}{4} & \frac{-3\pi}{4} & \frac{-\pi}{4} \end{bmatrix} \\
 1. \quad \text{Cosine} &= \frac{\sqrt{2}}{2} \begin{bmatrix} 1 & -1 & -1 & 1 \end{bmatrix}, \text{ which we can scale to} \\
 \text{Sine} &= \frac{\sqrt{2}}{2} \begin{bmatrix} 1 & 1 & -1 & -1 \end{bmatrix} \\
 \text{Cosine} &= \begin{bmatrix} 1 & -1 & -1 & 1 \end{bmatrix} \\
 \text{Sine} &= \begin{bmatrix} 1 & 1 & -1 & -1 \end{bmatrix} \\
 \\
 \text{Phase} &= \begin{bmatrix} 0 & \frac{\pi}{2} & \pi & \frac{-\pi}{2} \end{bmatrix} \\
 2. \quad \text{Cosine} &= \begin{bmatrix} 1 & 0 & -1 & 0 \end{bmatrix}, \\
 \text{Sine} &= \begin{bmatrix} 0 & 1 & 0 & -1 \end{bmatrix}
 \end{aligned}$$

- 15 In such cases, it is not only possible to generate easily the test signals, even if they need to be scaled, without having to use complex circuitry and look-up tables, but also operation of digital down mixer complex multiplier is greatly simplified. Multiplications turn into simple sign inversions.

$$Out_n = In_n \cdot LO_n$$

$$20 \quad \begin{cases} \text{Re}(Out_n) = \text{Re}(In_n) \cdot \cos_n - \text{Im}(In_n) \cdot \sin_n \\ \text{Im}(Out_n) = \text{Re}(In_n) \cdot \sin_n + \text{Im}(In_n) \cdot \cos_n \end{cases} \Rightarrow \begin{cases} \text{Re}(Out_n) = \pm \text{Re}(In_n) \mp \text{Im}(In_n) \\ \text{Im}(Out_n) = \pm \text{Re}(In_n) \pm \text{Im}(In_n) \end{cases}$$

Case 2 doesn't need any additions:

$$\begin{cases} \text{Re}(Out_n) = \pm \text{Re}(In_n) \\ \text{Im}(Out_n) = \pm \text{Im}(In_n) \end{cases} \quad \text{or} \quad \begin{cases} \text{Re}(Out_n) = \mp \text{Im}(In_n) \\ \text{Im}(Out_n) = \pm \text{Re}(In_n) \end{cases}$$

[0096] Because Out_n is then averaged and because it is required that components other than test tones needs to have a null average contribution, the number of measurements needs to be an entire multiple of LO number of phases, that is in the present case, multiple of 4.

[0097] An example of a possible implementation of this invention is given in Figure 6. It was chosen to consider case 2 presented in previous session, but a similar technique may apply to other cases. It is presented as a hardware block diagram, but may also be implemented in a simple microcontroller firmware (no need for FPU or emulation).

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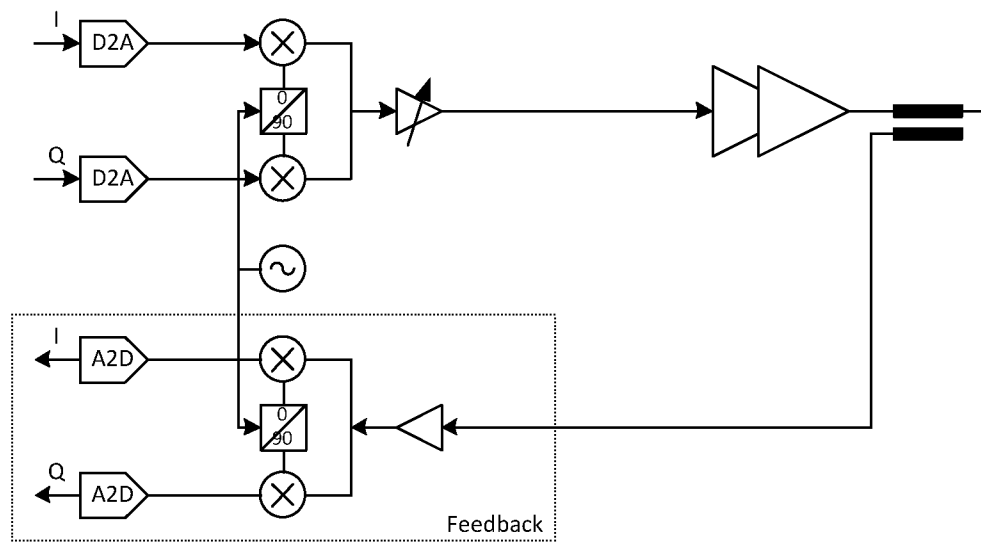
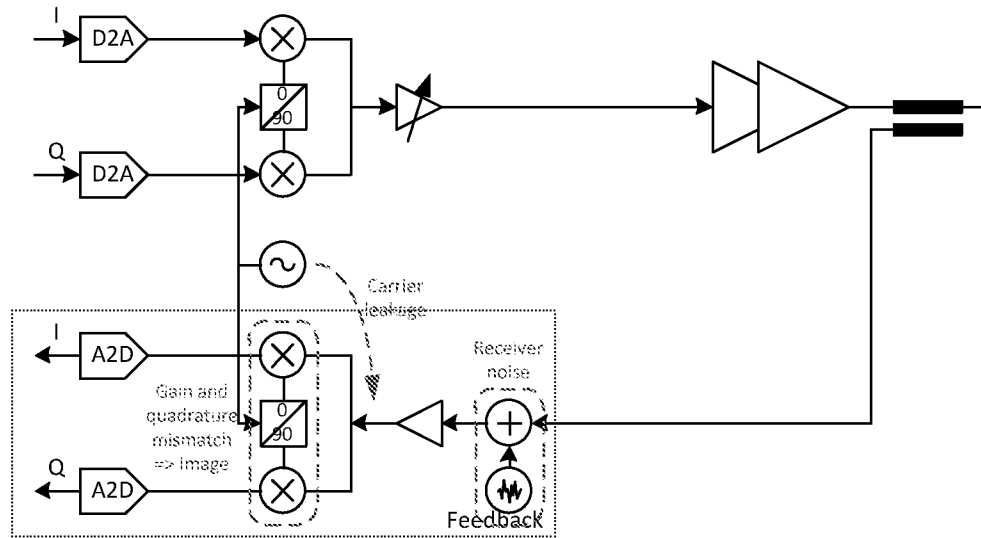
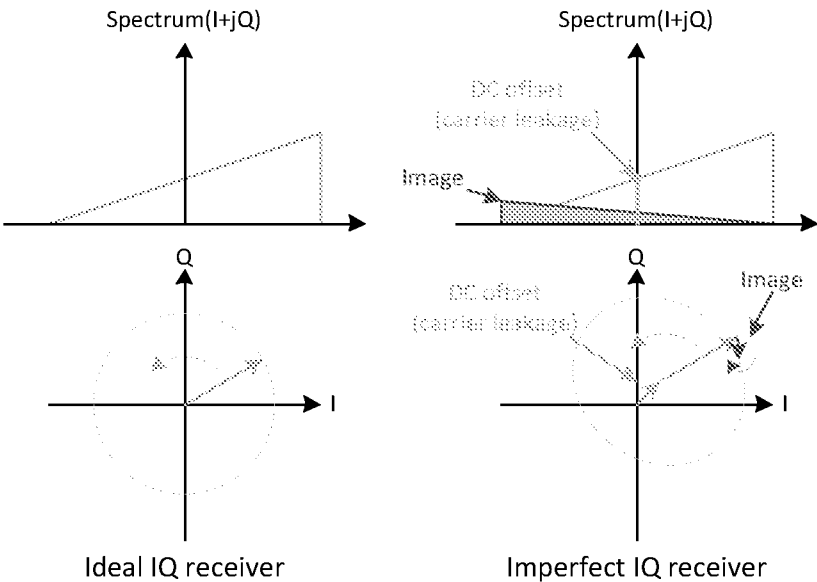
Figure 1 : Example of transmitter system using IQ feedback receiver

Figure 2 : IQ receiver impairments



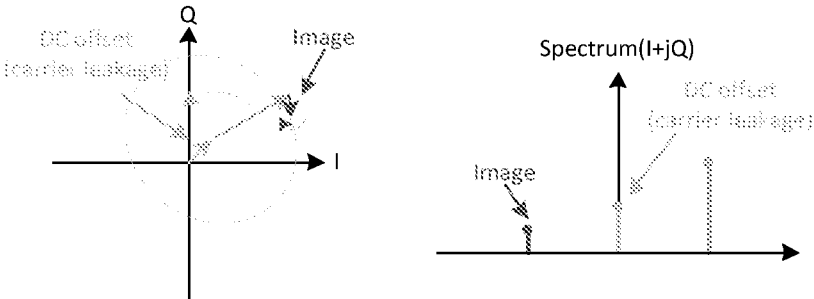
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Figure 3 : Vector and spectral effects of IQ receiver impairments



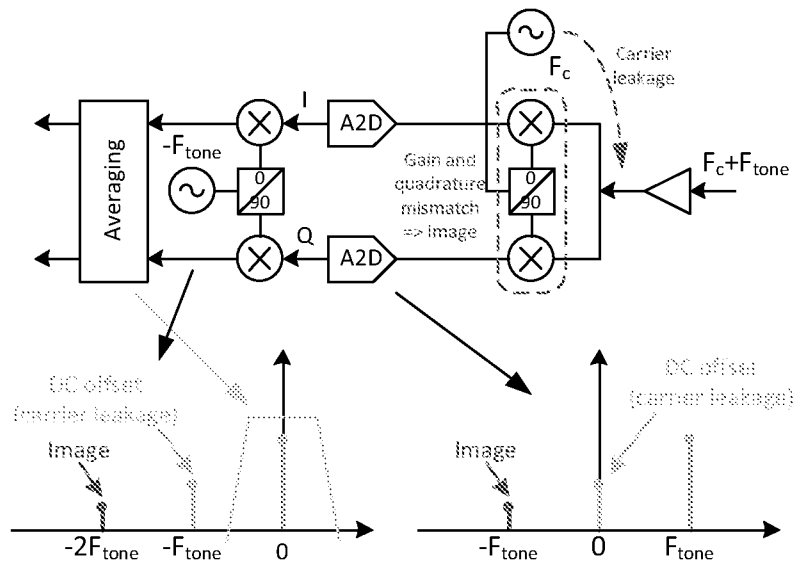
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Figure 4 : Frequency offset CW test signal



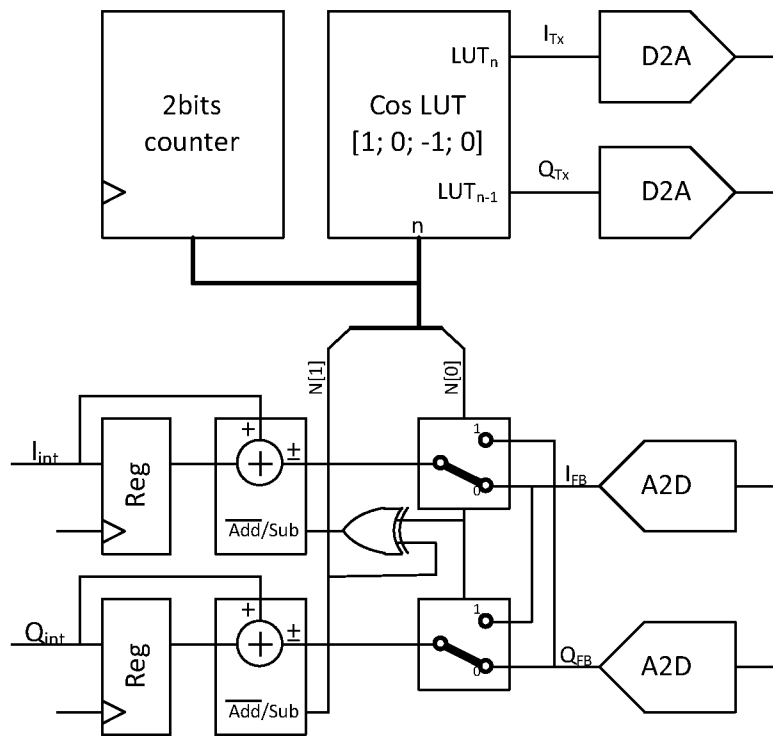
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Figure 5 : “Synchronous downmixing” of frequency offset CW test signal



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Figure 6 : One possible implementation



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Figure 7 : Pseudo code of one possible implementation

```

# Parameters...
magIQTx = xxx
nLoops = xxx
# Variables...
Iint = 0;
Qint = 0;
# Method implementation for "case 2"...
For l = 1 to 2^nLoops
    For m = 0 to 3
        # Set I and Q for test signal.
        Case (m)
            0:
                Itx = magIQTx
                Qtx = 0
            1:
                Itx = 0
                Qtx = magIQTx
            2:
                Itx = -magIQTx
                Qtx = 0
            3:
                Itx = 0
                Qtx = -magIQTx
        EndCase
        # If asynchronous implementation, optionally wait for
        # transmit and feedback signals to settle...
        Wait
        # Down convert and integrate I and Q...
        Case (m)
            0:
                Iint = Iint + Ifb
                Qint = Qint + Qfb
            1:
                Iint = Iint - Qfb
                Qint = Qint + Ifb
            2:
                Iint = Iint - Ifb
                Qint = Qint - Qfb
            3:
                Iint = Iint + Qfb
                Qint = Qint - Ifb
        EndCase
    EndFor
EndFor
# Average calculation...
Iint = Iint / ( 4 * 2^nLoops )
Qint = Qint / ( 4 * 2^nLoops )
# Can now calculate magnitude and/or phase...

```

Claims

What is claimed is:

1. Circuitry adapted to operate in one of a test mode and a normal
5 operating mode, and comprising:
 - an IQ to radio frequency modulator adapted to, during the test mode, modulate a quadrature radio frequency carrier signal using a quadrature test signal;
 - a radio frequency to IQ down-converter adapted to, during the test
10 mode, down-convert a down-converter radio frequency input signal to provide a quadrature down-converter output signal using the quadrature radio frequency carrier signal, such that the down-converter radio frequency input signal is based on the quadrature test signal and a complex gain of a transmit path; and
 - a digital frequency converter adapted to, during the test mode,
15 frequency convert the quadrature down-converter output signal to provide an averaged frequency converter output signal, which is a quadrature direct current signal that is representative of an amplitude and phase of the quadrature test signal and the
20 complex gain of the transmit path, such that the quadrature down-converter output signal is synchronized to the quadrature test signal.
2. The circuitry of claim 1 wherein a measured complex gain of the
25 transmit path is based on an amplitude of the quadrature test signal and a magnitude of the averaged frequency converter output signal.
3. The circuitry of claim 1 wherein the transmit path is an uplink path.
4. The circuitry of claim 1 wherein the IQ to radio frequency modulator is
30 further adapted to, during the normal operating mode, radio frequency modulate the quadrature radio frequency carrier signal using a quadrature transmit signal to provide a radio frequency modulator output signal to the transmit path.

5. The circuitry of claim 4 wherein, during the normal operating mode, the radio frequency modulator output signal is processed and forwarded to a radio frequency antenna via the transmit path.
6. The circuitry of claim 1 wherein during the test mode:
- 5
- the quadrature test signal has an in-phase test signal and a quadrature-phase test signal;
 - the in-phase test signal and the quadrature-phase test signal are both continuous wave signals;
 - an amplitude of the quadrature-phase test signal is about equal to

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 - an amplitude of the in-phase test signal; and
 - the quadrature-phase test signal is phase-shifted from the in-phase test signal by about 90 degrees.
7. The circuitry of claim 1 wherein the digital frequency converter comprises:
- 15
- a quadrature analog-to-digital converter adapted to, during the test mode, receive and analog-to-digital convert the quadrature down-converter output signal to provide a digital quadrature down-converter signal; and
 - a complex multiplier adapted to, during the test mode, receive and

20

 - multiply the digital quadrature down-converter signal and a quadrature local oscillator signal to provide a quadrature complex multiplier output signal, wherein multiplication of the digital quadrature down-converter signal and the quadrature local oscillator signal is a complex multiplication.
- 25
8. The circuitry of claim 7 wherein the digital frequency converter further comprises averaging circuitry adapted to, during the test mode, receive and average the quadrature complex multiplier output signal to provide the averaged frequency converter output signal.

9. The circuitry of claim 7 wherein the complex multiplier is further adapted to, during the test mode, function as a synchronous down-mixer of the quadrature test signal.
10. The circuitry of claim 7 wherein the complex multiplier is further adapted to, during the test mode, synchronize the quadrature down-converter output signal to the quadrature test signal.
11. The circuitry of claim 7 wherein:
- the quadrature local oscillator signal has an in-phase local oscillator signal and a quadrature-phase local oscillator signal;
 - during the multiplication of the digital quadrature down-converter signal and the quadrature local oscillator signal, a magnitude of the in-phase local oscillator signal is equal to one of 1, 0, and -1; and
 - during the multiplication of the digital quadrature down-converter signal and the quadrature local oscillator signal, a magnitude of the quadrature-phase local oscillator signal is equal to one of 1, 0, and -1.
12. The circuitry of claim 7 wherein:
- the quadrature local oscillator signal has an in-phase local oscillator signal and a quadrature-phase local oscillator signal;
 - the quadrature test signal has an in-phase test signal and a quadrature-phase test signal;
 - the quadrature-phase test signal is phase-shifted from the in-phase test signal by about 90 degrees;
 - the quadrature-phase local oscillator signal is phase-shifted from the in-phase local oscillator signal by about 90 degrees; and
 - the quadrature-phase test signal is phase-shifted from the quadrature-phase local oscillator signal by about 180 degrees.
13. The circuitry of claim 7 wherein:

- the quadrature test signal has an in-phase test signal and a quadrature-phase test signal;
 - each of the in-phase test signal and the quadrature-phase test signal is approximately a square wave; and
 - 5 • after each transition of the in-phase test signal and the quadrature-phase test signal, the multiplication of the digital quadrature down-converter signal and the quadrature local oscillator signal occurs after a steady-state of the digital quadrature down-converter signal is reached.
- 10 14. A method for measuring a complex gain of a transmit path comprising:
- modulating a quadrature radio frequency carrier signal using a quadrature test signal;
 - down-converting a down-converter radio frequency input signal to provide a quadrature down-converter output signal using the
 - 15 quadrature radio frequency carrier signal, such that the down-converter radio frequency input signal is based on the quadrature test signal and the complex gain of the transmit path;
 - frequency converting the quadrature down-converter output signal to provide an averaged frequency converter output signal, which
 - 20 is a quadrature direct current signal that is representative of an amplitude and phase of the quadrature test signal and the complex gain of the transmit path, such that the quadrature down-converter output signal is synchronized to the quadrature test signal; and
 - 25 • extracting the complex gain of the transmit path based on the amplitude and phase of the quadrature test signal and a magnitude and phase of the averaged frequency converter output signal.
- 30 15. The method of claim 14 wherein the frequency converting the quadrature down-converter output signal to provide the averaged frequency converter output signal comprises:

- providing and clearing an in-phase register and a quadrature-phase register;
- sampling an in-phase down-converter output signal and a quadrature-phase down-converter output signal using a quadrature analog-to-digital converter to obtain a first in-phase sample and a first quadrature-phase sample, respectively;
- adding the first in-phase sample to the in-phase register and adding the first quadrature-phase sample to the quadrature-phase register;
- sampling the in-phase down-converter output signal and the quadrature-phase down-converter output signal using the quadrature analog-to-digital converter to obtain a second in-phase sample and a second quadrature-phase sample, respectively;
- adding the second in-phase sample to the quadrature-phase register and subtracting the second quadrature-phase sample from the in-phase register;
- sampling the in-phase down-converter output signal and the quadrature-phase down-converter output signal using the quadrature analog-to-digital converter to obtain a third in-phase sample and a third quadrature-phase sample, respectively;
- subtracting the third in-phase sample from the in-phase register and subtracting the third quadrature-phase sample from the quadrature-phase register;
- sampling the in-phase down-converter output signal and the quadrature-phase down-converter output signal using the quadrature analog-to-digital converter to obtain a fourth in-phase sample and a fourth quadrature-phase sample, respectively;
- subtracting the fourth in-phase sample from the quadrature-phase register and adding the fourth quadrature-phase sample to the in-phase register; and
- forwarding contents of the in-phase register and the quadrature-phase register to averaging circuitry via an in-phase complex

multiplier output signal and a quadrature-phase complex multiplier output signal, respectively.

16. The method of claim 15 wherein the frequency converting the quadrature down-converter output signal to provide the averaged frequency converter output signal further comprises receiving and averaging a quadrature complex multiplier output signal to provide the averaged frequency converter output signal, such that the averaged frequency converter output signal has the in-phase complex multiplier output signal and the quadrature-phase complex multiplier output signal.
17. The method of claim 14 wherein the frequency converting the quadrature down-converter output signal to provide the averaged frequency converter output signal comprises:
- providing and clearing an in-phase register and a quadrature-phase register;
 - sampling an in-phase down-converter output signal and a quadrature-phase down-converter output signal using a quadrature analog-to-digital converter to obtain an in-phase sample and a quadrature-phase sample, respectively;
 - adding or subtracting the in-phase sample to or from, respectively, one of the in-phase register and the quadrature-phase register;
 - adding or subtracting the quadrature-phase sample to or from, respectively, another of the in-phase register and the quadrature-phase register;
 - repeating the sampling the in-phase down-converter output signal and the quadrature-phase down-converter output signal, the adding or subtracting the in-phase sample, and the adding or subtracting the quadrature-phase sample, as necessary; and
 - forwarding contents of the in-phase register and the quadrature-phase register to averaging circuitry via an in-phase complex multiplier output signal and a quadrature-phase complex multiplier output signal, respectively.

18. The method of claim 17 wherein the frequency converting the quadrature down-converter output signal to provide the averaged frequency converter output signal further comprises receiving and averaging a quadrature complex multiplier output signal to provide the averaged frequency converter output signal, such that the averaged frequency converter output signal has the in-phase complex multiplier output signal and the quadrature-phase complex multiplier output signal.
19. Circuitry adapted to operate in one of a test mode and a normal operating mode, and comprising:
- an IQ to radio frequency modulator adapted to, during the test mode, modulate a quadrature radio frequency carrier signal using a quadrature test signal; and
 - a radio frequency to IQ down-converter adapted to, during the test mode, down-convert a down-converter radio frequency input signal to provide a quadrature down-converter output signal using the quadrature radio frequency carrier signal, such that the down-converter radio frequency input signal is based on the quadrature test signal and a complex gain of a transmit path,
- wherein a digital frequency converter is adapted to, during the test mode, frequency convert the quadrature down-converter output signal to provide an averaged frequency converter output signal, which is a quadrature direct current signal that is representative of an amplitude and phase of the quadrature test signal and the complex gain of the transmit path, such that the quadrature down-converter output signal is synchronized to the quadrature test signal.
20. The circuitry of claim 19 wherein baseband facing circuitry comprises the digital frequency converter and the circuitry is antenna facing circuitry.

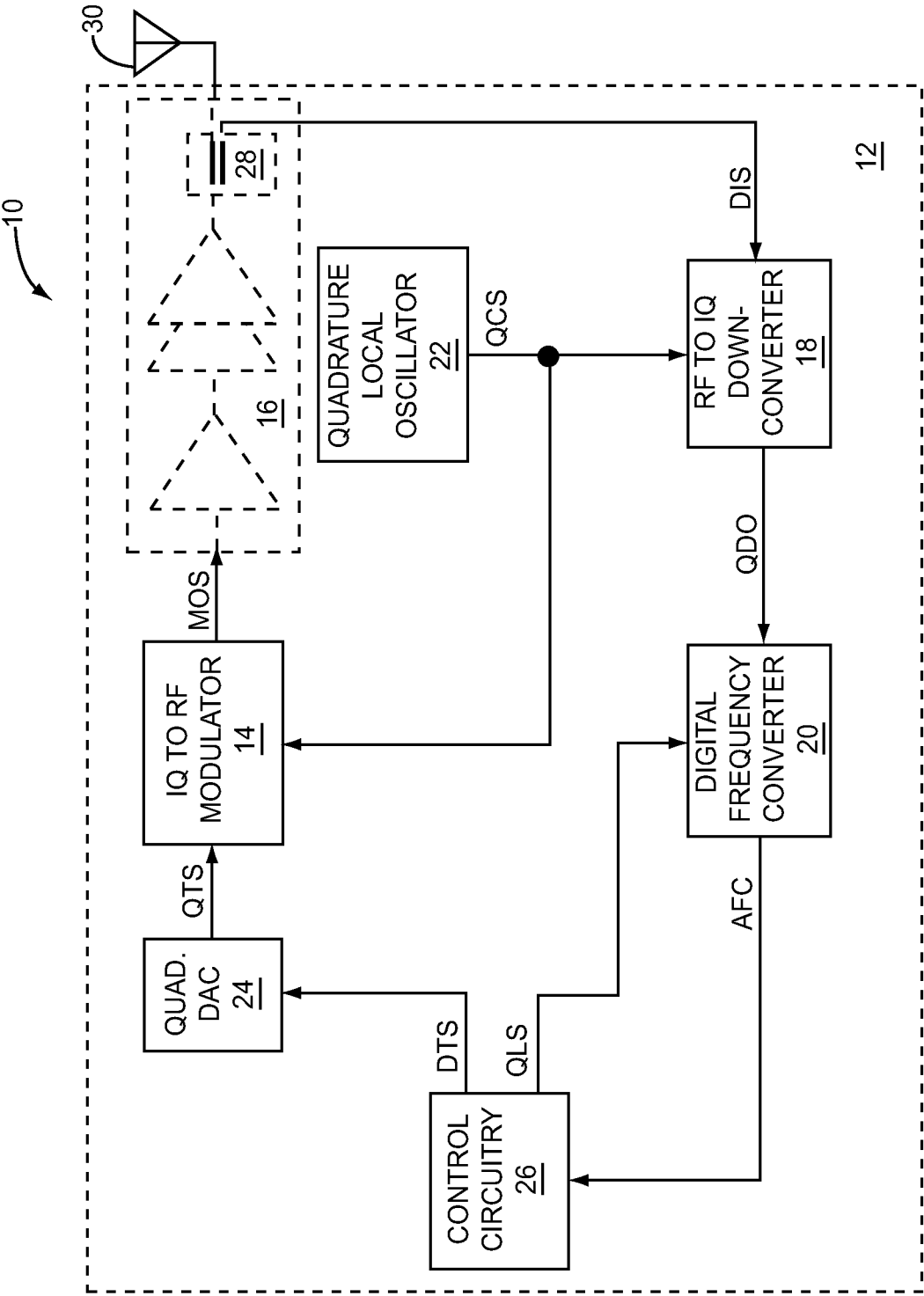


FIG. 1

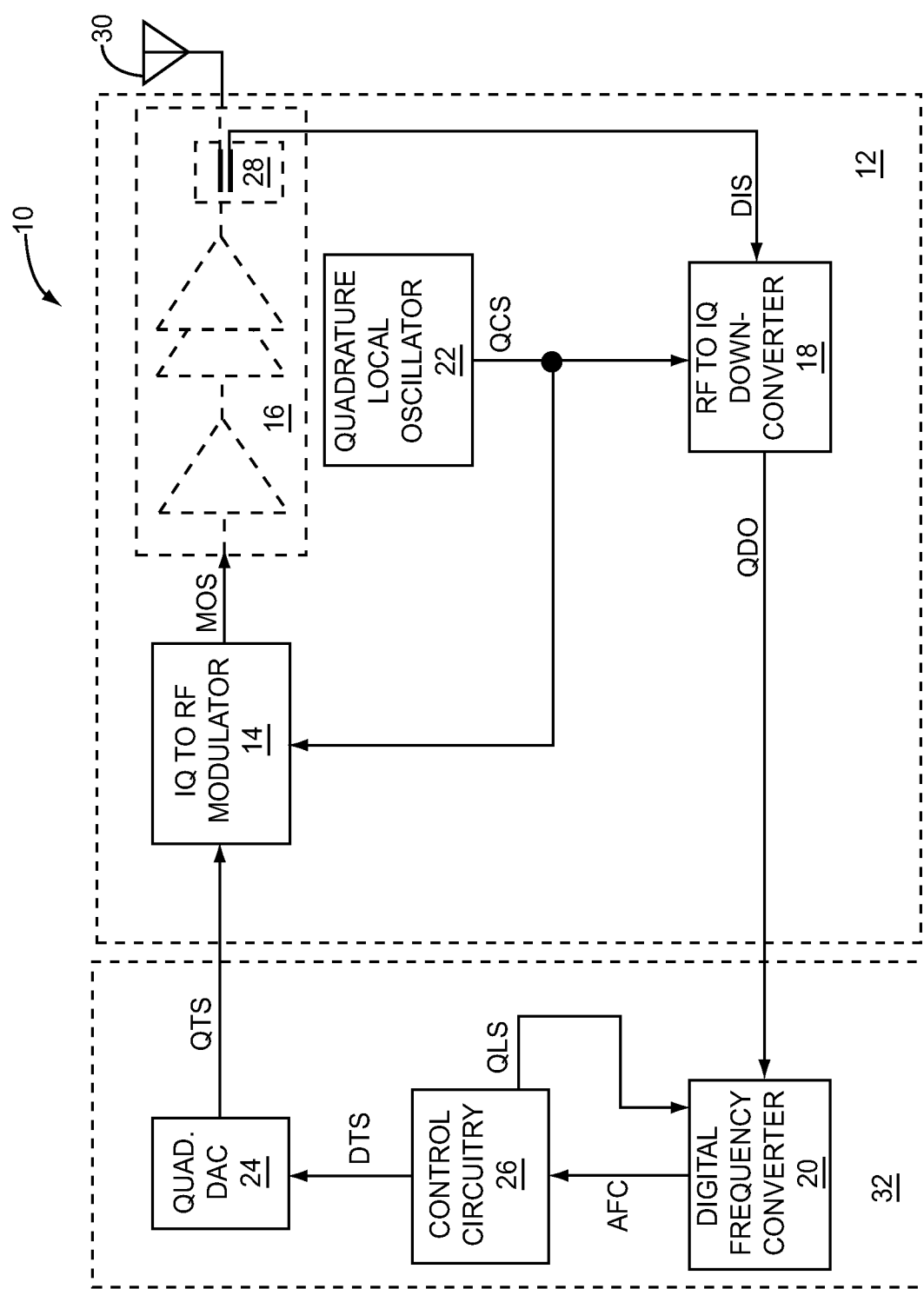


FIG. 2

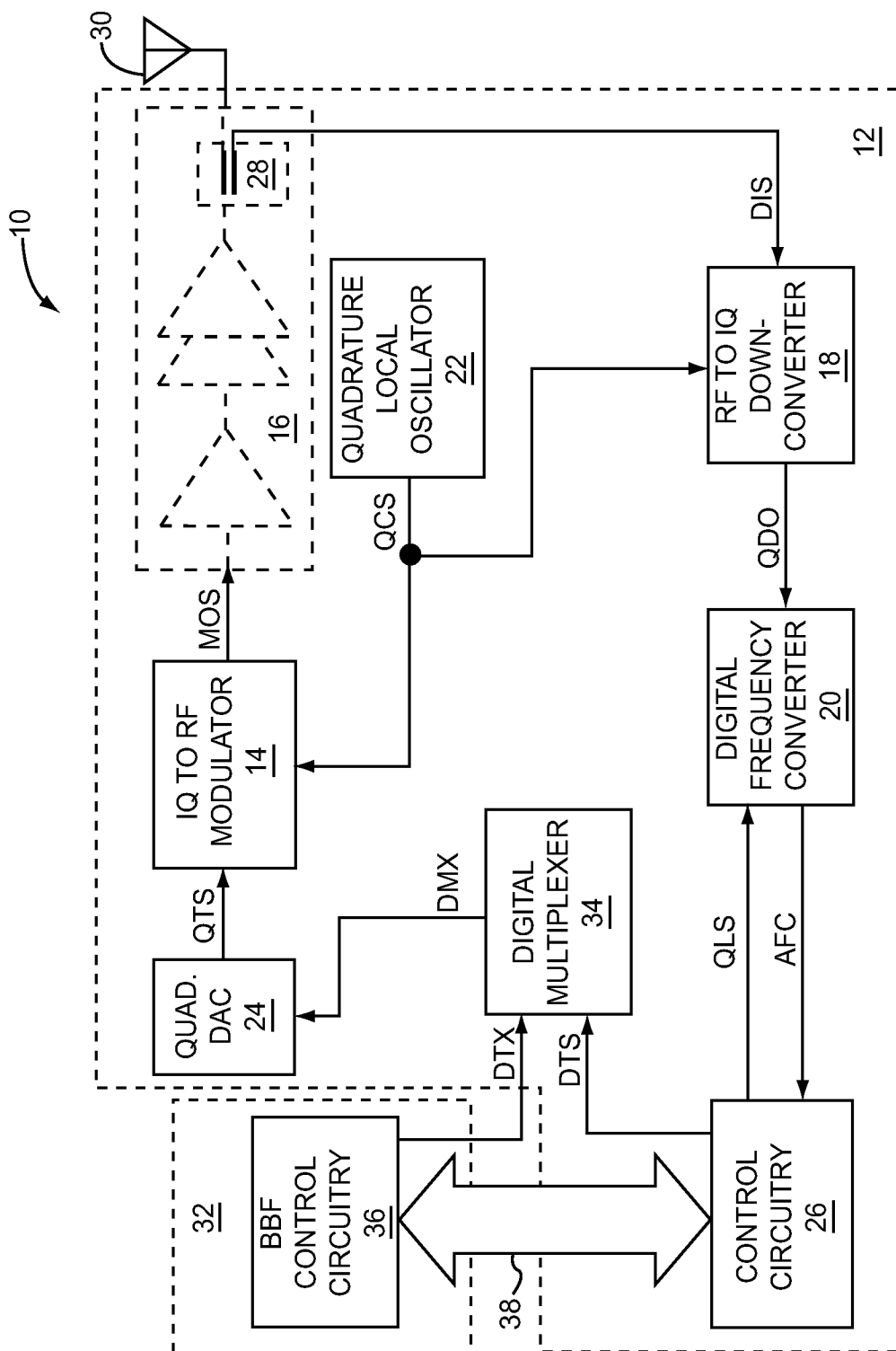


FIG. 3

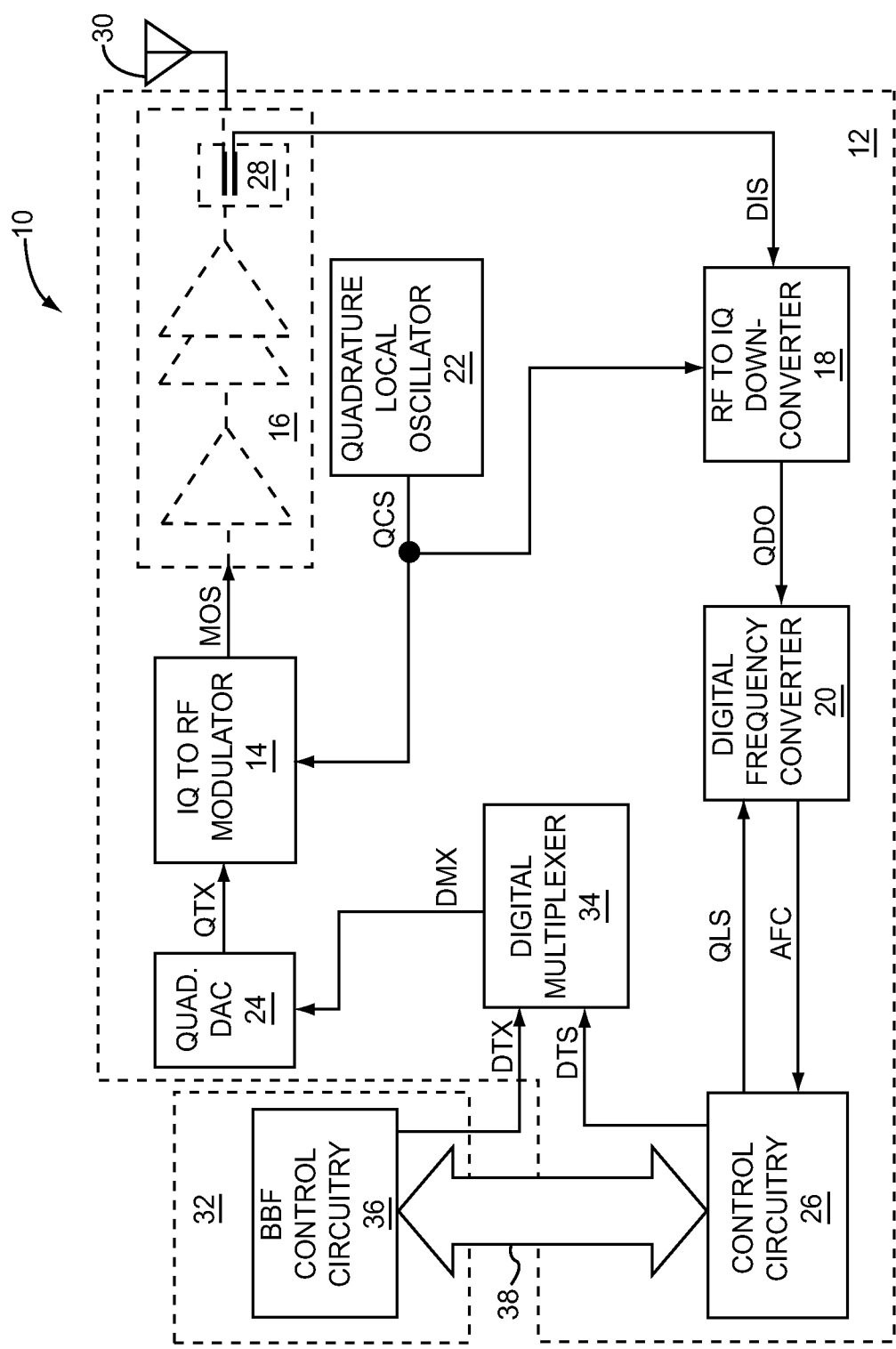


FIG. 4

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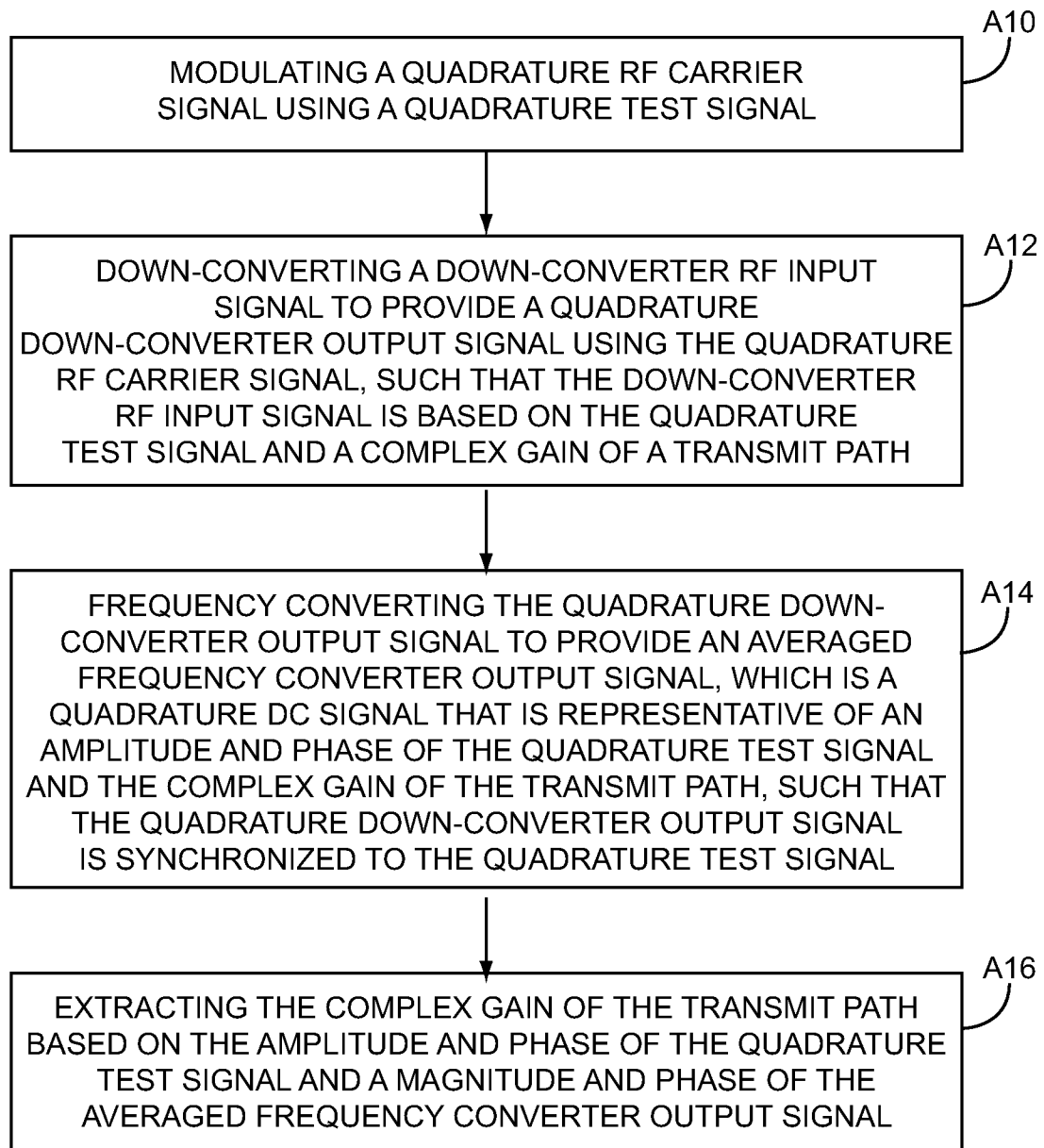


FIG. 5

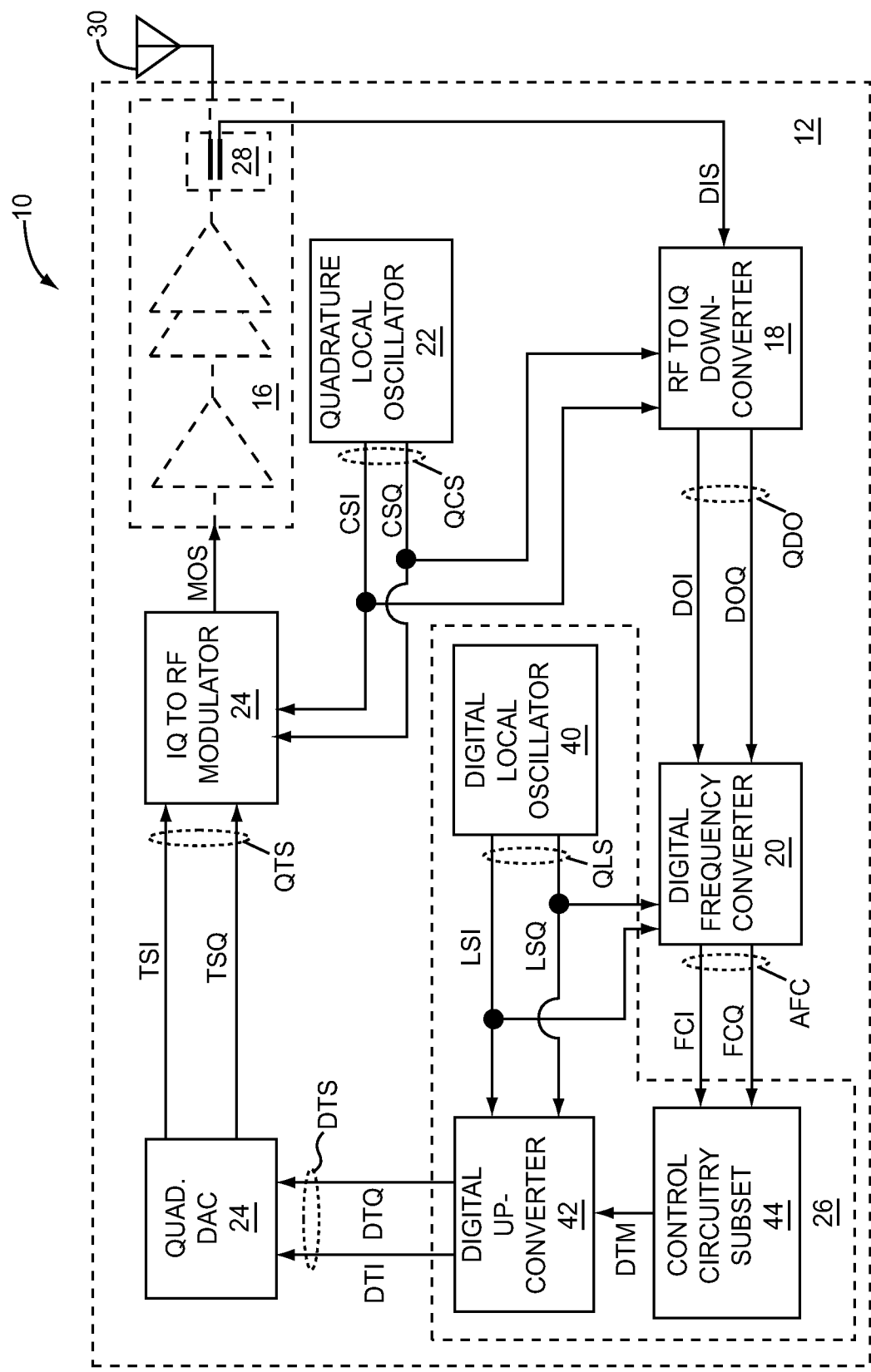


FIG. 6

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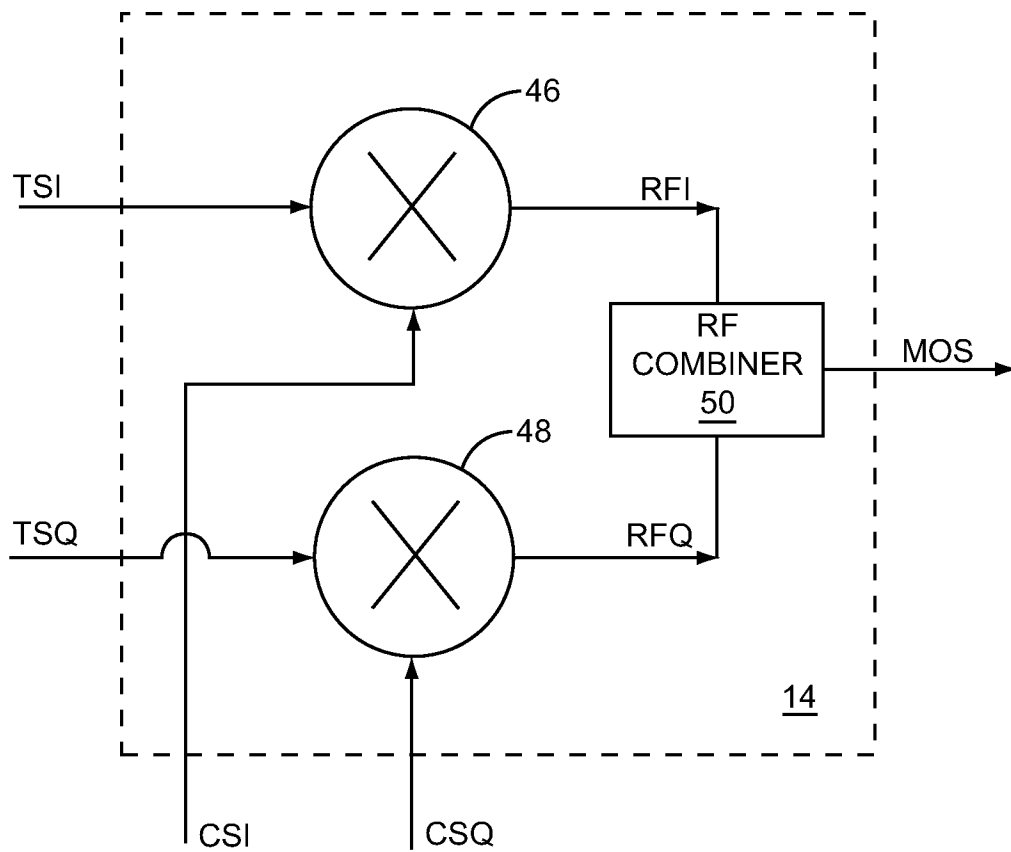


FIG. 7

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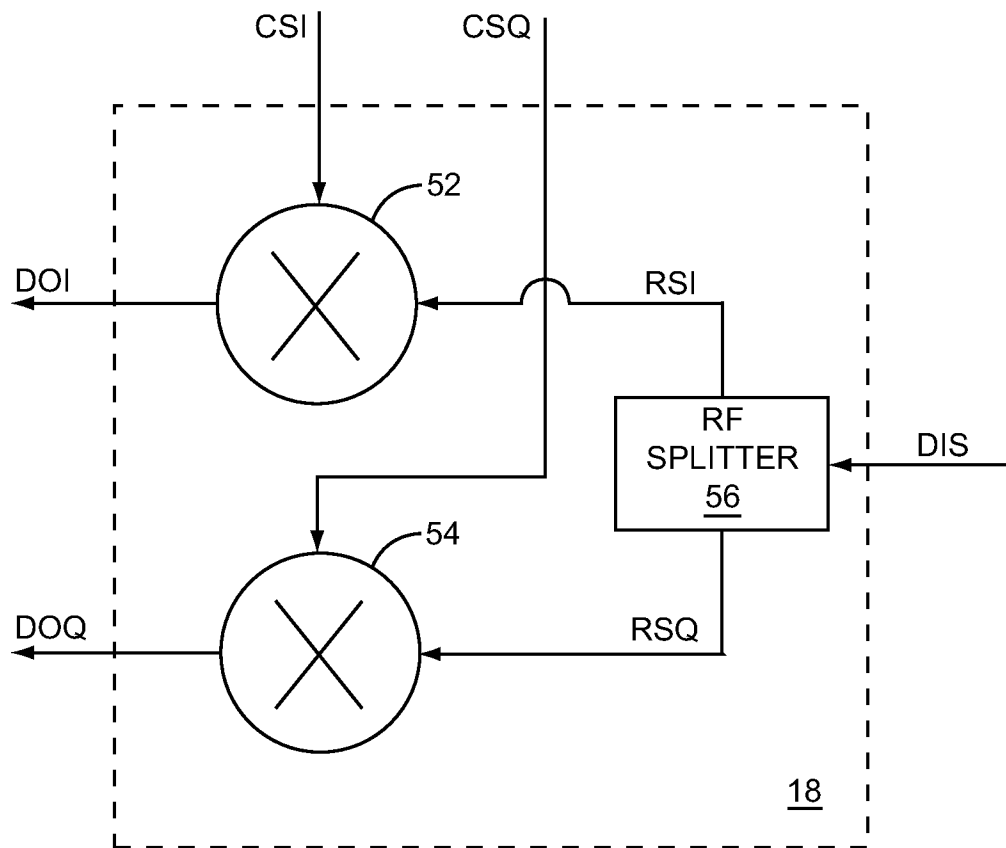


FIG. 8

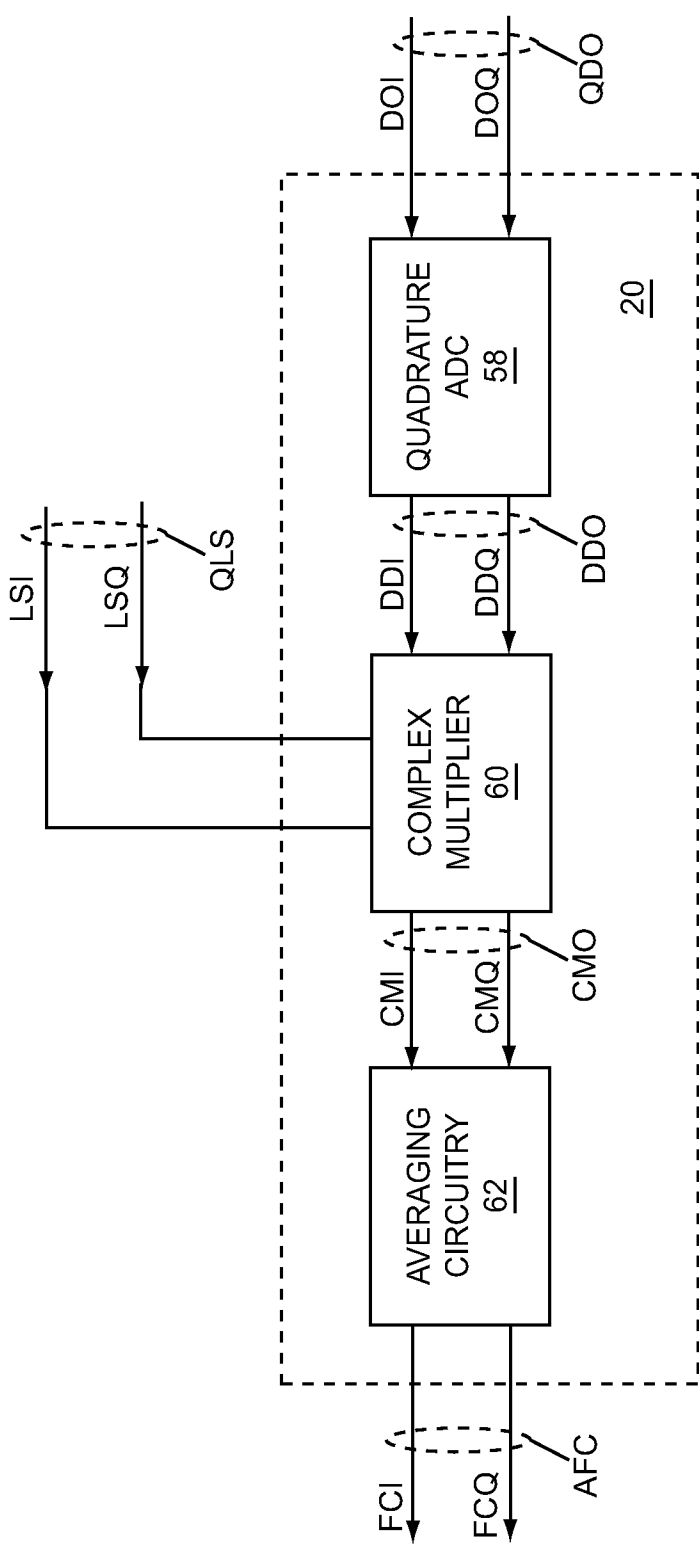
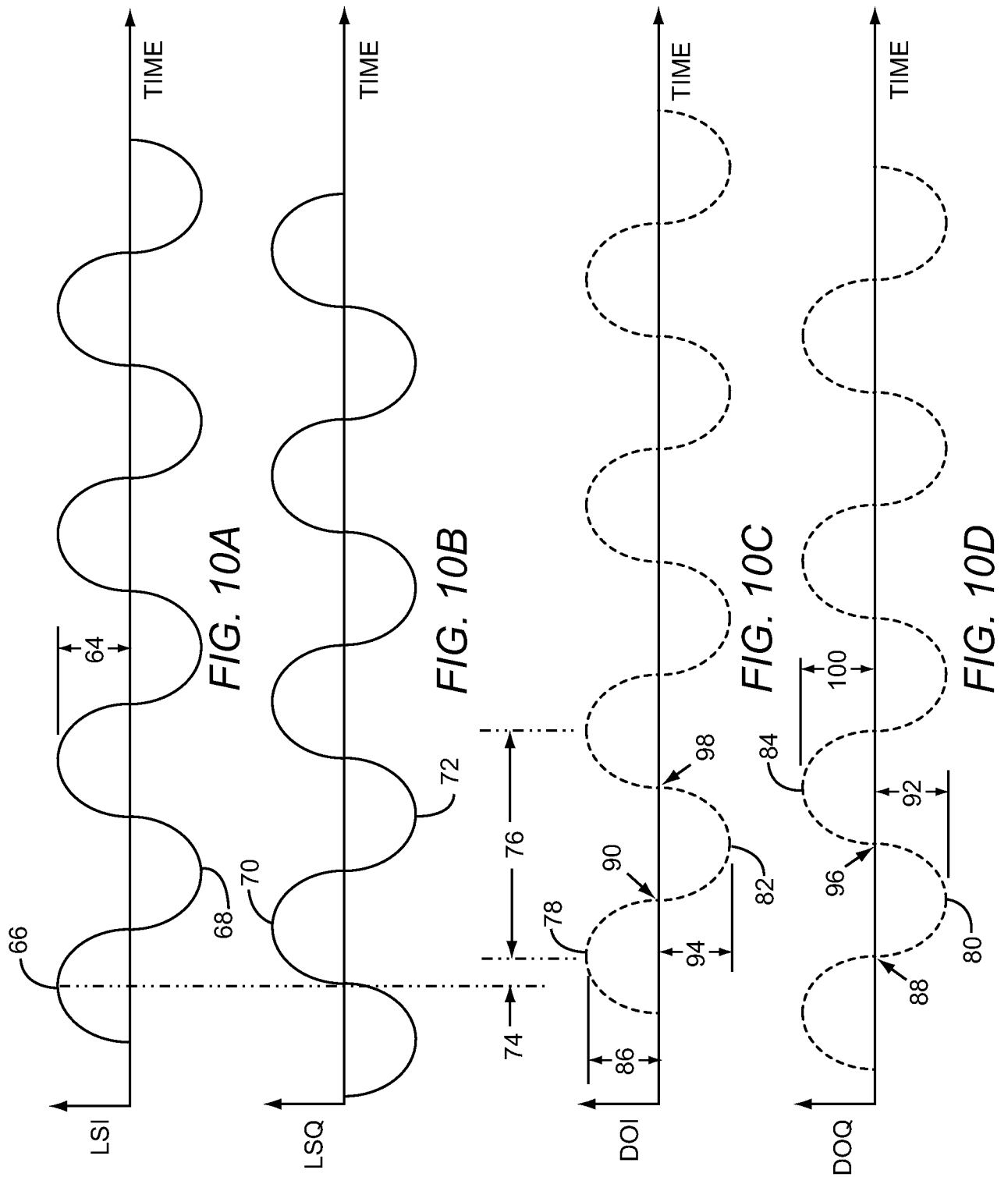
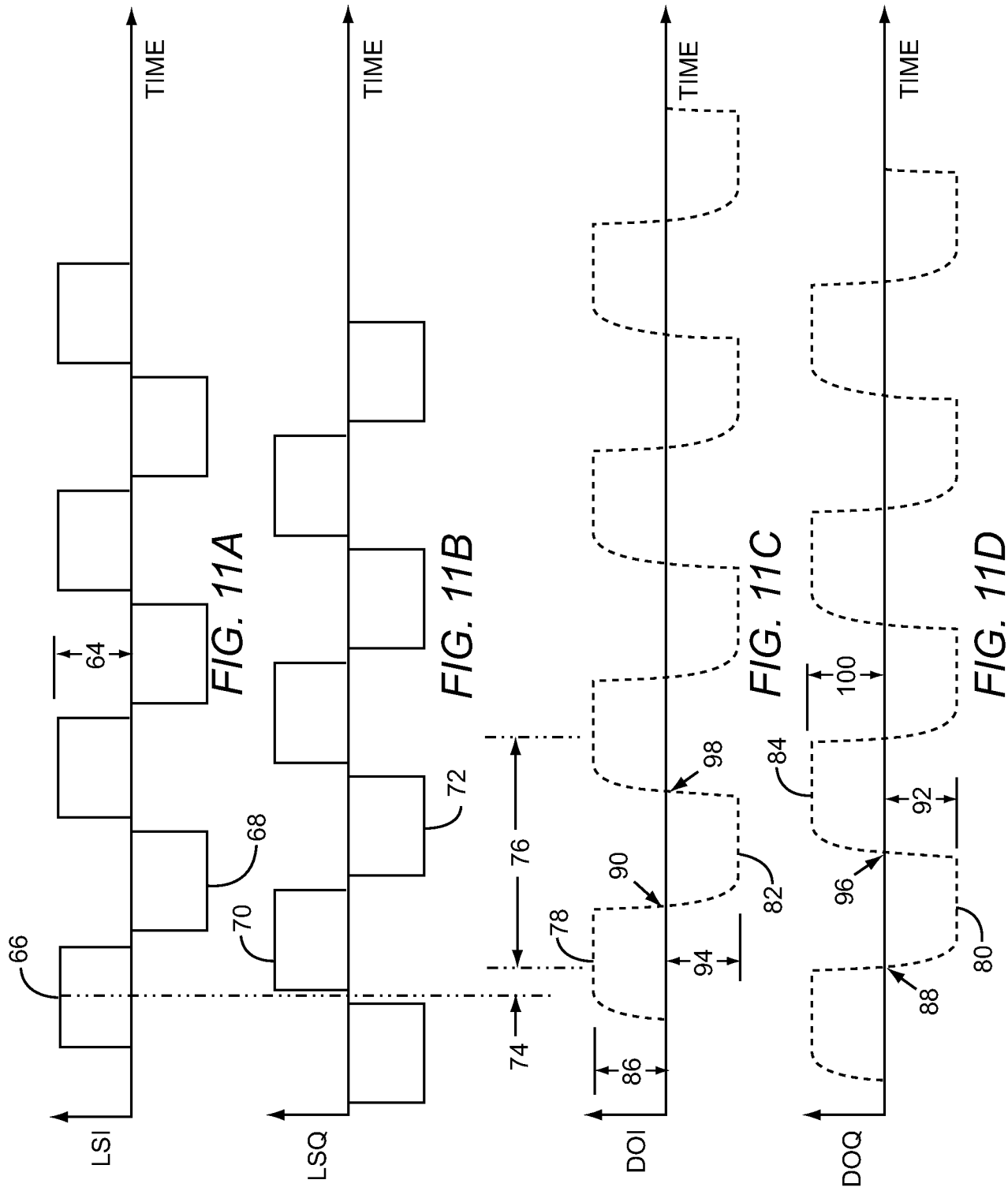


FIG. 9





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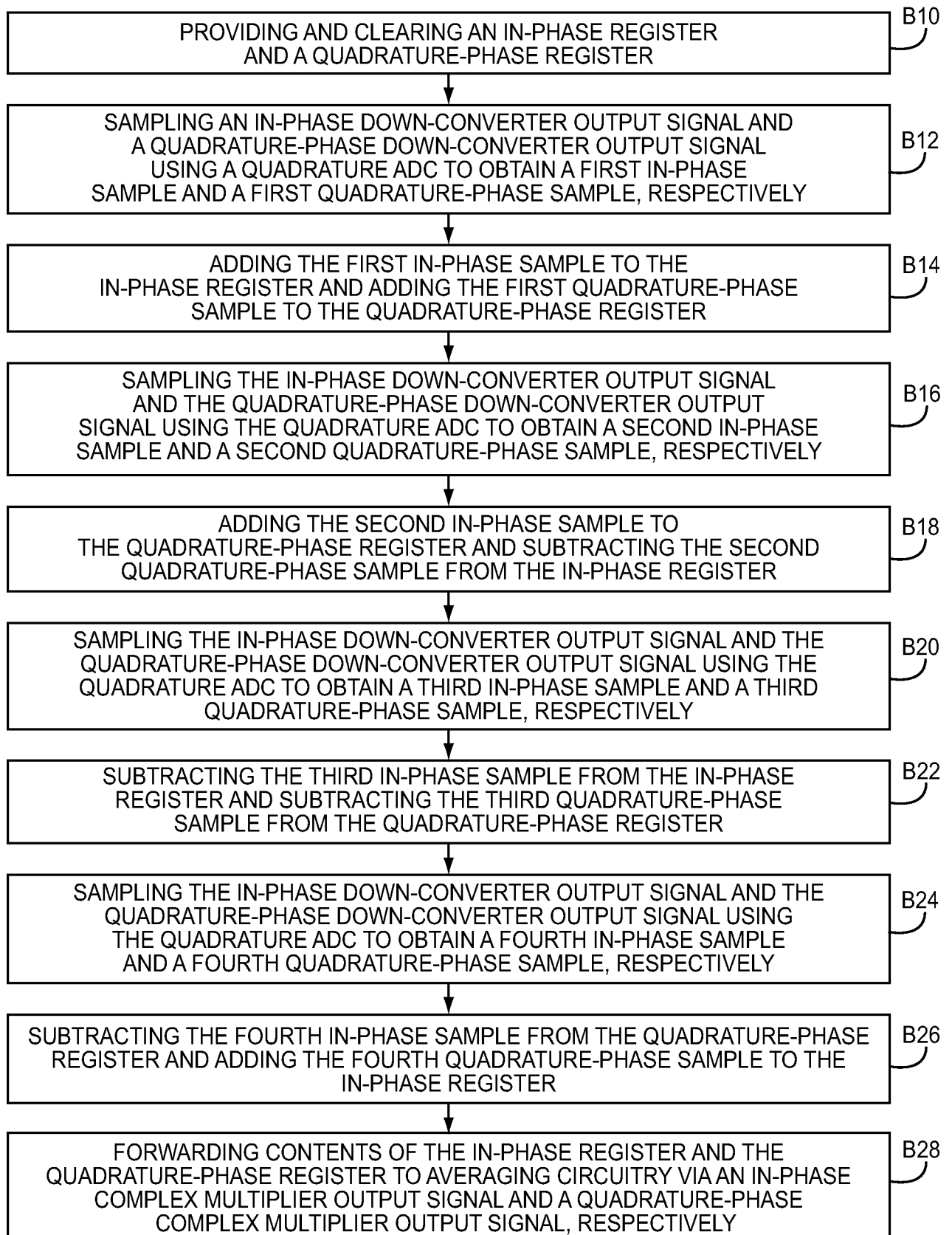
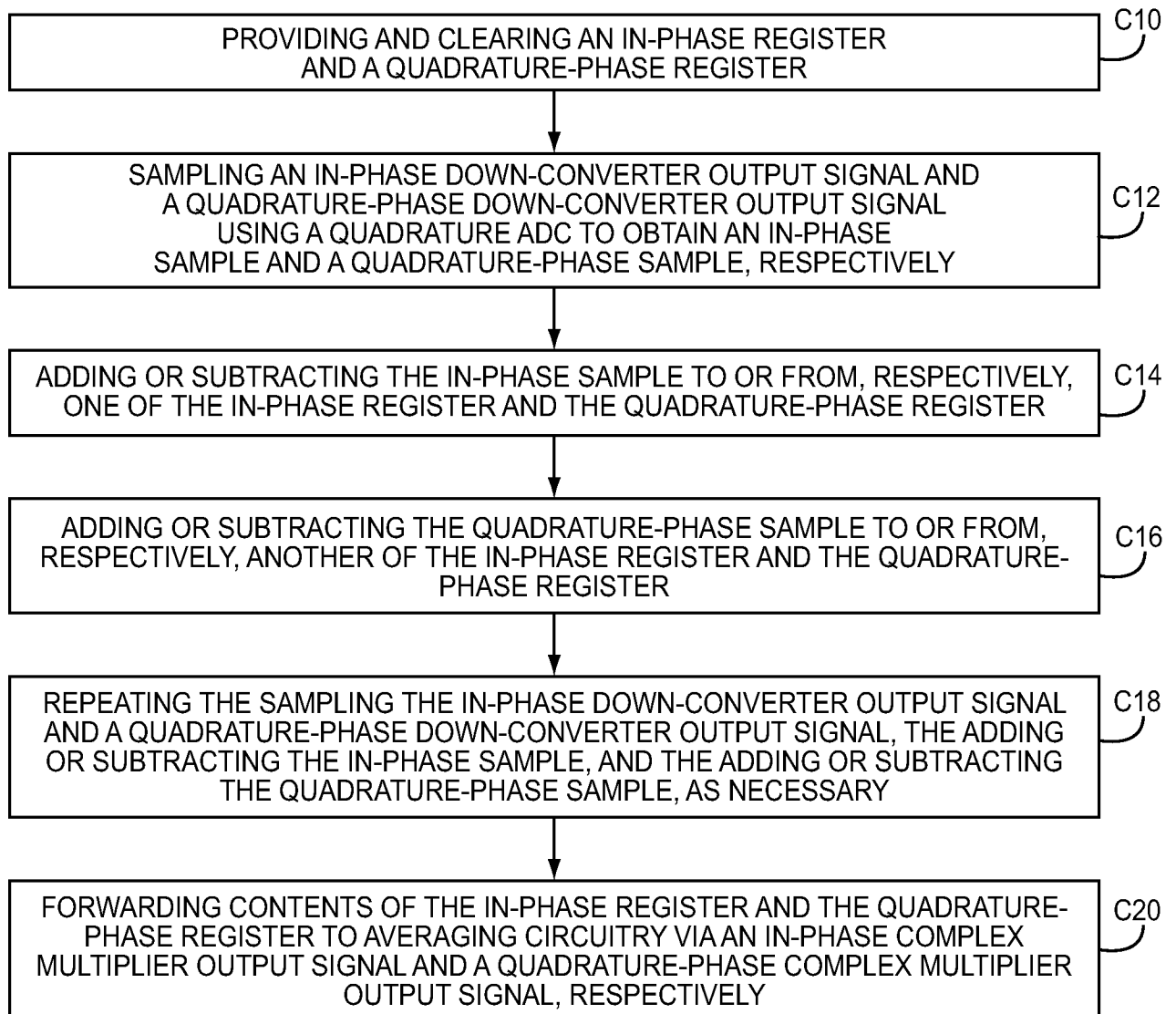


FIG. 12

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**FIG. 13**

INTERNATIONAL SEARCH REPORT

International application No.

PCT/US 12/40317

A. CLASSIFICATION OF SUBJECT MATTER

IPC(8) - H04B 1/44 (2012.01)

USPC - 455/78

According to International Patent Classification (IPC) or to both national classification and IPC

B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)
USPC: 455/78Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched
USPC: 455/78, 117, 118, 189.1, 190.1, 313, 323 (keyword limited - see terms below)Electronic data base consulted during the international search (name of data base and, where practicable, search terms used)
PubWEST (PGPB, USPT, USOC, EPAB, JPAB); GOOGLE; GoogleScholar; GooglePatents
Search Terms: receiver, wireless, transmit, amplitude, phase, frequency, modulation, quadrature, testing, mode, converting, down-converting, complex, gain, quadrature, averaging, multiplying, radio, RF, IQ, circuit, synchronize

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	US 2008/0280577 A1 (Beukema et al.) 13 November 2008 (13.11.2008), entire document, especially abstract, para. [0027]-[0029], [0040], [0041]	1 - 20
A	US 2003/0206603 A1 (Husted) 06 November 2003 (06.11.2003), entire document, especially abstract	1 - 20
A	US 2011/0018626 A1 (Kojima) 27 January 2011 (27.01.2011), entire document, especially abstract, para. [0045]	1 - 20
A	US 2010/0321127 A1 (Watanabe et al.) 23 December 2010 (23.12.2010), entire document, especially abstract, para. [0132]	1 - 20
A	US 2005/0157778 A1 (Trachewsky et al.) 21 July 2005 (21.07.2005), entire document, especially abstract, para. [0041], [0071]	1 - 20

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Date of the actual completion of the international search

15 August 2012 (15.08.2012)

Date of mailing of the international search report

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