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(54) **PHASE SHIFTING DEVICE**

PHASENSCHIEBERANORDNUNG

DISPOSITIF DE DECALAGE DE PHASE

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(73) Proprietors:
• **NIHON DENGYO KOSAKU CO. LTD.**
Tokyo 101 (JP)
• **NTT MOBILE COMMUNICATIONS NETWORK**
INC.
Minato-ku, Tokyo 105-8436 (JP)

(72) Inventors:
• **EBINE, Yoshio**
Yokohama-shi, Kanagawa 235 (JP)

• **KARIKOMI, Masahiro**
Kawagoe-shi, Saitama 350 (JP)
• **MATSUOKA, Tohru**
Zama-shi, Kanagawa 228 (JP)

(74) Representative:
Luderschmidt, Schüler & Partner GbR
Patentanwälte,
Postfach 3929
65029 Wiesbaden (DE)

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Description

TECHNICAL FIELD

[0001] The present invention relates to a phase shifting device used in, for example, a transmitting device capable of high output through parallel operation of a plurality of transmitters and a power supply apparatus for directional control of antennas.

BACKGROUND ART

[0002] When attempting to vary the direction of maximum radiation or side lobe characteristic of an array antenna by appropriately controlling the driving phase of each of a plurality of radiating elements forming the array antenna, or when attempting to realize a high-output transmitting device by parallel-operating a plurality of transmitters and controlling the output phase of each transmitter such that each is the same phase, line stretchers constructed so as to mechanically vary the length of the transmission line of a signal, or waveguide-type phase shifting devices formed by inserting a dielectric plate within a waveguide have conventionally been used.

[0003] Fig. 1 presents several views of a waveguide-type phase shifting device of the prior art, Fig. 1A showing a plan view, Fig. 1B showing a side view, Fig. 1C showing a sectional view taken at the B-B line of Fig. 1B, and Fig. 1D showing a sectional view taken at the A-A line of Fig. 1A.

[0004] In rectangular waveguide 11, flanges 12₁ and 12₂ are provided for inserting and connecting such a waveguide-type phase shifting device within a rectangular waveguide circuit. A dielectric plate 13 is provided within rectangular waveguide 11 such that the plate surface is parallel to the electric field within the waveguide 11. As shown in Fig. 1D, the contour of this dielectric plate 13 is formed as a parallelogram, this parallelogram having inclines on the edges of the radio-wave incident side and edges of the opposite side which are formed so as to improve the radio-wave reflection characteristic at these edge portions.

[0005] Instead of providing inclines to the edges of the radio-wave incident side and edges of the opposite side of this dielectric 13, the radio-wave incident portion and opposite side portion of the dielectric 13 may be formed such that the plate thickness gradually varies.

[0006] Support fittings 14₁ and 14₂ for dielectric plate 13 pass through the opposing short sides of rectangular waveguide 11 and dielectric plate 13. Support fittings 14₁ and 14₂ may freely slide at the portions where they pass through the opposing short sides of rectangular waveguide 11 but are secured to the portions where they pass through dielectric plate 13.

[0007] Coupling plate 15 links together support fittings 14₁ and 14₂. This coupling plate 15 serves as a handle for moving support fittings 14₁ and 14₂ either forward or backward in the axial direction of each of support fittings 14₁ and 14₂ while maintaining dielectric plate 13 in the attitude shown in Fig. 1D, thus allowing the plate surfaces of dielectric plate 13 to be moved from a position coinciding with the central axis in the longitudinal direction of rectangular waveguide 11 to a position close to either of the opposing short sides as shown in Fig. 1C, thus enabling variation in the proportion of shift change of radio waves propagated through rectangular waveguide 11.

[0008] In other words, such a phase shifting device uses the change in propagation speed of radio waves within rectangular waveguide 11 according to the dielectric constant, thickness, and length in the direction of wave propagation of dielectric plate 13. When interposed at a position coinciding with the central axis in the longitudinal direction of rectangular waveguide 11, where the electric field intensity is at maximum strength, dielectric plate 13 exercises a large effect upon the propagation speed of radio waves, but the electric field strength progressively weakens with distance from the longitudinal central axis of the rectangular waveguide 11 and proximity to either of the short sides, and consequently, as the position of insertion of dielectric plate 13 shifts away from the central axis of rectangular waveguide 11 and approaches either of the short sides, the effect upon the propagation speed of radio waves decreases. Accordingly, the degree of phase shifting can be varied by changing the position of insertion of dielectric plate 13.

[0009] Support fittings 14₁ and 14₂ are maintained parallel to each other, their relative spacing (spacing in relation to the longitudinal direction of rectangular waveguide 11) being selected as $\lambda_g/4$ (λ_g is the wavelength within the waveguide corresponding to the employed frequency), whereby reflected waves arising at the support fitting 14₁ closer to the radio-wave-incident portion and reflected waves arising at support fitting 14₂ which travel back to the position of support fitting 14₁ are of mutually reversed phase and cancel each other, thereby enabling an improved reflection characteristic.

[0010] A line stretcher used in the prior art must regulate the line length according to the required degree of phase shifting, and therefore, when the required degree of phase shifting is great, not only is a large-scale mechanical structure required, but a relatively time-consuming and labor-intensive adjustment is required to accurately match the line length with the degree of phase shift.

[0011] The waveguide-type phase shifting device shown in Fig. 1 involves the drawbacks that a long dielectric plate

13 is required when a large amount of phase shift is called for, resulting in a phase shifting device of large overall size, and that a great deal of time and effort is required to adjust the insertion point of the dielectric plate 13 to accurately match the amount of phase shift with the required value.

[0012] Fig. 2 shows a power supply circuit configured using phase shifting devices of the prior art for controlling the driving phase of subarray antennas and for varying the direction of maximum radiation as well as the side lobe characteristic of an array antenna. This power supply circuit is configured from subarray antennas 16₁-16₄ each composed of a plurality of element antennas, phase shifting devices 17₁-17₃ of the above-described prior art, transmission lines 18₁-18₃ having a degree of phase shift that serves as a standard, and two-branch circuits 19₁-19₃.

[0013] A phase shifting device of the prior art not only entails the same drawbacks as the above-described line stretcher, but when used as shown in Fig. 2, in which a power supply circuit is configured for varying the direction of maximum radiation or side lobe characteristic of an array antenna, further entails the drawback of complex structure of the power supply circuit due to the need for transmission lines 18₁-18₃ having an amount of phase shift that serves as a standard and two-branch circuits 19₁-19₃ for phase shifting devices 17₁-17₃, respectively.

DISCLOSURE OF THE INVENTION

[0014] The object of the present invention is to provide a phase shifting device which has a simple and compact structure, and which allows easy adjustment at the time of manufacture and easy handling during use. GB-A-2 005 083 discloses a phase shifter for use at microwave frequencies comprising a first antenna arranged to emit circularly polarized waves from the microwave source and the second antenna for receiving the waves, the antennae being mounted for relative axial rotation. If signals must be transmitted efficiently from the first to the second antenna, then the size of the antenna has to be increased to an extent of few wavelengths to decrease the amount of leakage, resulting in failure provide a compact phase shifting device.

DISCLOSURE OF THE INVENTION

[0015] The object of the present invention is to provide a phase shifting device which has a simple and compact structure, and which allows easy adjustment at the time of manufacture and easy handling during use.

[0016] The present invention provides a phase shifting device with the features of claim 1.

[0017] The two-partition output of the two-partition circuit, which distributes the input power in two portions having a mutual phase difference of substantially 90°, is applied to the first microwave antenna means, which generates from its front surface a circularly polarized wave. This circularly polarized wave couples at the second antenna means, and the two outputs of the second antenna means arising from this coupled circularly polarized wave are combined at the combining circuit. In the following the first and second microwave antenna means are designated as first and second drives, respectively. When the first and second drivers are rotated relative to each other around the axis that joins the centers of each of the first and second drivers, the phase difference between the input of the two-partition circuit that applies driver power to the first driver and the combined output of the second driver varies in accordance with this rotation.

[0018] This phase shifting device allows variation of the degree of phase shift over a range of from 0° to 360°, and moreover, has a simple and compact structure that enables extremely easy adjustment at the time of manufacture and service during use. In addition, the relation between relative angle of rotation of the two sealed cases and the degree of phase shift is proportional, and therefore, the degree of phase shift can be read directly if graduations of degrees are added around the circumference of one of the sealed cases and a pointer is added at a point on the circumference of the other sealed case.

[0019] Furthermore, the present invention provides a phase shifting device with the features of claim 7.

[0020] When the first driver is driven, linearly polarized waves are generated from the front surface of the driver, and the two orthogonal components of this linearly polarized wave are coupled at the second driver. When the first and second drivers are rotated relative to each other around the axis joining the centers of each of the first and second drivers, the phase difference between the input applied to the first driver and either of the two outputs of the combining circuit to which the two outputs of the second driver are applied varies according to the angle of rotation; and in addition, the phase difference between the two outputs of the combining circuit to which the two outputs of the second driver are applied also varies according to the relative angle of rotation between the first and second drivers.

[0021] This phase shifting device allows variation of the degree of phase shift over a range of from 0° to 360°, and moreover, has a simple and compact structure and enables extremely easy adjustment at the time of manufacture and handling during use. In addition, the relation between relative angle of rotation of the two sealed cases and the degree of phase shift is proportional, and therefore, the degree of phase shift can be read directly if graduations of degrees are added around the circumference of one of the sealed cases and a pointer is added at a point on the circumference of the other sealed case.

[0022] This phase shifting device is well-suited for control of the direction of maximum radiation or side lobe characteristics of an array antenna because it both allows variation of the phase difference between the input and either one of the two outputs of the combining circuit according to the relative angle of rotation between the sealed cases, and moreover, allows variation of the phase difference between the two outputs according to the relative angle of rotation between the sealed cases.

BRIEF DESCRIPTION OF THE DRAWING

[0023]

Figs. 1A - 1D show an example of a waveguide-type phase shifting device of the prior art;
 Fig. 2 shows an example of the use of the prior-art phase shifting device shown in Fig. 1;
 Fig. 3 is a side view of a phase shifting device according to an embodiment of the present invention;
 Fig. 4 is a side view of a coupler 21 shown in Fig. 3;
 Fig. 5 is a plan view of coupler shown in Fig. 3;
 Fig. 6 is a sectional view taken at line C-C of Fig. 4;
 Fig. 7 is a sectional view taken at line D-D of Fig. 5;
 Fig. 8 illustrates the operation of the phase shifting device according to the embodiment of Fig. 3;
 Fig. 9 shows the return loss characteristic in coaxial connection plug 21_{31} of the phase shifting device of the embodiment shown in Fig. 3;
 Fig. 10 shows the transmission loss characteristic between coaxial connection plugs 21_{31} and 21_{34} of the phase shifting device of the embodiment shown in Fig. 3;
 Fig. 11 shows the degree of phase shift in relation to the relative angle of rotation ϕ between sealed cases 21_1 and 21_2 in the phase shifting device of the embodiment shown in Fig. 3;
 Fig. 12 shows the transmission loss characteristic between input terminal 22_1 and output terminal 24_1 in the phase shifting device of the embodiment shown in Fig. 3;
 Fig. 13 is a sectional view showing the principal parts of a phase shifting device according to another embodiment of the present invention;
 Fig. 14 is a sectional view showing the principal parts of a phase shifting device according to another embodiment of the present invention;
 Fig. 15 is a block diagram showing a phase shifting device according to the embodiment of Fig. 13;
 Fig. 16 is a side view of a phase shifting device according to another embodiment of the present invention;
 Fig. 17 is a side view of coupler 31 within Fig. 16;
 Fig. 18 is a plan view of coupler 31 within Fig. 16;
 Fig. 19 is a sectional view taken at line G-G of Fig. 17;
 Fig. 20 is a sectional view taken at line H-H of Fig. 17;
 Fig. 21 is a sectional view taken at line I-I of Fig. 18;
 Figs. 22A and 22B show the electric field level produced by drive element 31 and the outputs E_1 and E_2 of 90° 3-dB hybrid circuit 32 in the phase shifting device of Fig. 16;
 Fig. 23 shows the reflection characteristic in coaxial connection plug 31_{31} of the phase shifting device of Fig. 16;
 Fig. 24 shows the transmission loss characteristic between coaxial connection plugs 31_{31} and 31_{33} of the phase shifting device of Fig. 16;
 Fig. 25 shows the degree of phase shift in relation to the relative angle of rotation ϕ between sealed cases 31_1 and 31_2 in the phase shifting device of Fig. 16;
 Fig. 26 shows the observation results of the transmission loss between coaxial connection plug 31_{31} of coupler 31 and the output terminal 32_3 of 90° 3-dB hybrid circuit 32, and between coaxial connection plug 31_{31} of coupler 31 and output terminal 32_4 of 90° 3-dB hybrid circuit 32;
 Fig. 27 shows an example of the use of both outputs E_2 and E_1 of output terminals 32_3 and 32_4 of 90° 3-dB hybrid circuit 32; and
 Fig. 28 is a sectional view showing the principal parts of the phase shifting device according to another embodiment of the present invention.

DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

[0024] Fig. 3 is a side view of the phase shifting device according to an embodiment of the present invention.

[0025] The phase shifting device according to this embodiment is constructed from coupler 21 which includes cylindrical sealed cases 21_1 and 21_2 which are each closed at one end, and terminals 21_{31} - 21_{34} made up of coaxial connection plugs; 90° 3-dB hybrid circuit 22 which is composed of a directional coupler including input terminal 22_1 , isolation

terminal 22₂, and output terminals 22₃ and 22₄; reflectionless terminator 23 connected to isolation terminal 22₂; 90° 3-dB hybrid circuit 24 which is composed of a directional coupler including output terminal 24₁, isolation terminal 24₂, and input terminals 24₃ and 24₄; reflectionless terminator 25 connected to isolation terminal 24₂; coaxial cable 26₁ connecting output terminal 22₄ and terminal 21₃₁; coaxial cable 26₂ connecting output terminal 22₃ and terminal 21₃₂; coaxial cable 27₁ connecting terminal 21₃₄ and input terminal 24₃; and coaxial cable 27₂ connecting terminal 21₃₃ and input terminal 24₄.

[0026] Here, the output power of each of output terminals 22₃ and 22₄ is 1/2 of the input power to input terminal 22₁, and, for example, the phase of the output of output terminal 22₃ is substantially 90° delayed with respect to the phase of the output of output terminal 22₄. Furthermore, inputs of equivalent magnitude are applied to each of input terminals 24₃ and 24₄, the input to input terminal 24₃ being, for example, substantially 90° advanced with respect to the phase of input to input terminal 24₄.

[0027] The lengths of each of coaxial cables 26₁ and 26₂ are adjusted such that the phase of the output of output terminal 22₃ of 90° 3-dB hybrid circuit 22 is delayed substantially 90° with respect to the phase of the output of output terminal 22₄, and moreover, such that both outputs are applied to input coaxial connection plugs 21₃₁ and 21₃₂ of coupler 21 while being kept in a mutually equivalent relation. The lengths of coaxial cables 27₁ and 27₂ are each adjusted such that the outputs from output coaxial connection plugs 21₃₃ and 21₃₄ of coupler 21 are applied to the input terminals 24₃ and 24₄ of 90° 3-dB hybrid circuit 24 with the phase difference and the equal amplitude relation between the outputs maintained unchanged.

[0028] Fig. 4 shows a side view of coupler 21 of Fig. 3, Fig 5 shows a plan view of the sealed case 21₁ side of coupler 21 as seen from the bottom side, Fig. 6 is an enlarged sectional view taken along line C-C of Fig. 4, and Fig. 7 is an enlarged sectional view taken along line D-D of Fig. 5.

[0029] As can be clearly seen from Fig. 7, stepped portions are formed in the side walls at the end portions of the openings of both of sealed cases 21₁ and 21₂, the end portion of the opening of sealed case 21₂ fitting inside the end portion of the opening of sealed case 21₁, the two sealed cases 21₁ and 21₂ being coupled together as a unit, and sealed cases 21₁ and 21₂ being constructed so as to allow rotation relative to each other around their cylindrical axis.

[0030] Sealed cases 21₁ and 21₂ are manufactured by first machining a metal block or press-forming a metal sheet in the prescribed shape; by forming a suitable synthetic resin in a preliminary form of the prescribed shape and subsequently applying a metal film to the surface by a electroless plating or vacuum evaporation process; or by multilayer stacking of dielectric plates having an appropriate dielectric constant and forming as a cylinder with one closed end that shields electromagnetic energy in accordance with Snell's law.

[0031] Coaxial connection plugs 21₃₁ and 21₃₂ each include internal conductors 21₄₁ and 21₄₂. A round insulation plate 21₅₁ composed of a material having excellent highfrequency characteristics and a thickness less than the transmission wavelength such as an organic material such as polyethylene or fluorinated ethylene or an inorganic material such as a ceramic is adhered to the inner surface of the bottom wall of sealed case 21₁ using a suitable adhesive. Metal plate 21₆₁ is secured to the surface of round insulation plate 21₅₁ using a suitable adhesive, and in addition, portions of the periphery of metal plate 21₆₁ are connected to internal conductors 21₄₁ and 21₄₂ of coaxial connection plugs 21₃₁ and 21₃₂, and the first driver composed of a microstrip antenna is formed with sealed case 21₁ on the opposite side of round insulation plate 21₅₁ as the ground conductor, metal plate 21₆₁ as the first driver element, and the contact points between metal plate 21₆₁ and interior conductors 21₄₁ and 21₄₂ of coaxial connection plugs 21₃₁ and 21₃₂ as the driver points.

[0032] As can be seen from Fig. 6, a right angle is formed by the straight line joining the center of metal plate 21₆₁ and the driving point constituted by the contact point between metal plate 21₆₁ and the interior conductor 21₄₁ of coaxial connection plug 21₃₁ and the straight line joining the center of metal plate 21₆₁ and the driving point constituted by the contact point between metal plate 21₆₁ and the internal conductor 21₄₂ of coaxial connection plug 21₃₁.

[0033] In addition, the exterior conductors of each of coaxial connection plugs 21₃₁ and 21₃₂ are electrically connected to sealed case 21₁, and as shown in Fig. 7, a portion of sealed case 21₁ has been removed around the periphery of internal conductor 21₄₁ to form a gap such that internal conductor 21₄₁ makes no mechanical contact with sealed case 21₁, and a gap is similarly formed in sealed case 21₁ at the portion around the periphery of internal conductor 21₄₂.

[0034] As the method for securing metal plate 21₆₁ to the surface of round insulation plate 21₅₁, a setscrew in the center of metal plate 21₆₁ (the portion wherein electric field intensity is 0) may also be used to secure the plate to round insulation plate 21₅₁ rather than an adhesive, or metal plate 21₆₁ may be screwed at its center to the bottom wall of sealed case 21₁ through round insulation plate 21₅₁.

[0035] Instead of using metal plate 21₆₁, the driver element of the microstrip antenna making up the first driver may be formed by applying a metal film to the surface of round insulation plate 21₅₁ by a process such as vacuum evaporation and finishing to the required outline shape by a process such as etching.

[0036] Whether the driver element is formed from a metal plate or metal film, its outline shape may instead of a circle be formed as a square, electrical connection with the internal conductors 21₄₁ and 21₄₂ of coaxial connection plugs 21₃₁ and 21₃₂ being effected in the corner portions of the square.

[0037] Next will be explained the dimensions of driver element 21₆₁ for a case in which driver element 21₆₁ is driven in basic mode. When the outline shape of driver element 21₆₁ is formed as a circle as shown in Fig. 6, if the specific inductive capacity of round insulation plate 21₅₁ is ϵ_r and the design frequency is f_0 , the radius of driver element 21₆₁ is preferably selected as substantially $1.841 C/(2\pi \cdot f_0 \cdot \epsilon_r^{1/2})$, and when the outline shape of driver element 21₆₁ is formed as a square, the length of one side of driver element 21₆₁ is preferably selected as substantially $C/(2f_0 \cdot \epsilon_r^{1/2})$ (C being the speed of light).

[0038] Next, in Fig. 7, 21₄₃ and 21₄₄ are the internal conductors of coaxial connection plugs 21₃₃ and 21₃₄, respectively, 21₅₂ is a round insulation plate, and 21₆₂ is the second driver element; the material, method of fabrication, and mutual electrical and mechanical relation of each of these parts being identical to the material, method of fabrication, and mutual electrical and mechanical relation of each of respective coaxial connection plugs 21₃₁ and 21₃₂, internal conductors 21₄₁ and 21₄₂, round insulation plate 21₅₁, and first driver element 21₆₁ on the side of sealed case 21₁.

[0039] Fig. 8 illustrates the operation of this phase shifting device. The input power E applied to the input terminal of 90° 3-dB hybrid circuit 22 is distributed into two substantially equal portions and outputted from output terminals 22₃ and 22₄, the phase of output E₁ of output terminal 22₃ being delayed substantially 90° with respect to the phase of output E₂ of output terminal 22₄.

[0040] Output is outputted to isolation terminal 22₂ according to the difference between the impedance viewing the load side from output terminal 22₃ and the impedance viewing the load side from output terminal 22₄, and this output is absorbed by reflectionless terminator 23; however, in a state in which output terminal 22₃ and the load are matched and output terminal 22₄ and the load are matched, the output outputted to isolation terminal 22₂ becomes extremely small, and as a result, the permissible power of reflectionless terminator 23 may be extremely low.

[0041] Output E₁ of output terminal 22₃ of 90° 3-dB hybrid circuit 22 is applied by way of coaxial cable 26₂ to the driver point at which internal conductor 21₄₂ of coaxial connection plug 21₃₂ of coupler 21 connects to first driver element 21₆₁. The instantaneous value of the electric field propagated from this driving point in the Z direction (the X-axis and Y-axis are determined as shown in Fig. 6, and the direction perpendicular to the X- and Y-axis is the Z direction) is E_X. Output E₂ of output terminal 22₄ of 90° 3-dB hybrid circuit 22 is applied by way of coaxial cable 26₁ to the driver point at which internal conductor 21₄₁ of coaxial connection plug 21₃₁ of coupler 21 is connected to first driver element 21₆₁, and the instantaneous value of the electric field propagated in the Z direction from this driver point is E_Y. The instantaneous values E_X and E_Y of the electric field are:

$$E_1 = -j \frac{E}{\sqrt{2}} \equiv E_X$$

$$E_2 = \frac{E}{\sqrt{2}} \equiv E_Y$$

[0042] The electric field propagated in the Z direction couples at the second driver element 21₆₂, which together with round insulation plate 21₅₂ and the bottom wall of the second sealed case 21₂ forms the second driver; but if the angle formed between the straight line joining the center of first driver element 21₆₁ with the driver point at which internal conductor 21₄₁ of coaxial connection plug 21₃₁ of coupler 21 connects to first driver element 21₆₁ and the straight line joining the center of second driver element 21₆₂ with the driver point at which internal conductor 21₄₄ of coaxial connection plug 21₃₄ of coupler 21 connects to second driver element 21₆₂ is represented by ϕ , the output of coaxial connection plug 21₃₄ is represented by E₃, and the output of coaxial connection plug 21₃₃ is represented by E₄, the outputs E₃ and E₄ are:

$$E_3 = E_Y \cos \phi - E_X \sin \phi$$

$$E_4 = E_Y \sin \phi - E_X \cos \phi$$

[0043] The output E₃ of coaxial connection plug 21₃₄ is applied through input terminal 24₃ to 90° 3-dB hybrid circuit 24, and output E₄ of coaxial connection plug 21₃₃ is applied through input terminal 24₄ to 90° 3-dB hybrid circuit 24. If the output of isolation terminal 24₂ of 90° 3-dB hybrid circuit 24 is represented by E₅, and the output of output terminal 24₁ is represented by E₆, outputs E₅ and E₆ are respectively:

$$\begin{aligned}
E_5 &= \frac{E_3}{\sqrt{2}} - j \frac{E_4}{\sqrt{2}} \\
&= \frac{1}{\sqrt{2}} \left\{ \frac{E}{\sqrt{2}} \cos \phi + j \frac{E}{\sqrt{2}} \sin \phi \right\} \\
&\quad - j \frac{1}{\sqrt{2}} \left\{ \frac{E}{\sqrt{2}} \sin \phi - j \frac{E}{\sqrt{2}} \cos \phi \right\} \\
&= 0
\end{aligned}$$

$$\begin{aligned}
E_6 &= \frac{E_3}{\sqrt{2}} + \frac{E_4}{\sqrt{2}} \\
&= -j \frac{1}{\sqrt{2}} \left\{ \frac{E}{\sqrt{2}} \cos \phi + j \frac{E}{\sqrt{2}} \sin \phi \right\} \\
&\quad + \frac{1}{\sqrt{2}} \left\{ \frac{E}{\sqrt{2}} \sin \phi - j \frac{E}{\sqrt{2}} \cos \phi \right\} \\
&= E \sin \phi - j E \cos \phi \\
&= E \cos \left(\frac{\pi}{2} - \phi \right) - j E \sin \left(\frac{\phi}{2} - \phi \right) \\
&= E \exp \left\{ -j \left(\frac{\pi}{2} - \phi \right) \right\}
\end{aligned}$$

[0044] In other words, in this phase shifting device, the phase of the output of output terminal 24₁ of 90° 3-dB hybrid circuit 24 can be shifted by ϕ with respect to the phase of the input to input terminal 22₁ of 90° 3-dB hybrid circuit 22 by simply rotating the sealed cases 21₁ and 21₂ with respect to each other by the angle ϕ .

[0045] Fig. 9 shows the reflection characteristics at coaxial connection plug 21₃₁ for a case in which the inside diameter of the cylinders having one closed end that form sealed cases 21₁ and 21₂ of coupler 21 are selected as $0.285 \lambda_0$ (λ_0 being the free space wavelength corresponding to the designed frequency f_0), the distance between the bottom wall of sealed case 21₁ and the bottom wall of sealed case 21₂ is set at $0.089 \lambda_0$, the specific inductive capacity of each of round insulation plates 21₅₁ and 21₅₂ is set at 10, the dielectric dissipation factor of each of round insulation plates 21₅₁ and 21₅₂ is set at 0.0055, the thickness of round insulation plates 21₅₁ and 21₅₂ is set at $0.023 \lambda_0$, and each of the first and second driver elements 21₆₁ and 21₆₂ are formed in a circular shape of diameter $0.21 \lambda_0$. Here, the axis of abscissas shows the relative frequency with respect to the design frequency f_0 , and the axis of ordinates shows the amount of return loss (dB).

[0046] Fig. 10 shows the transmission characteristics between coaxial connection-plugs 21₃₁ and 21₃₄ for a case in which each of the dimensions of coupler 21 is the same as for Fig. 9, the axis of abscissas being equivalent to Fig. 9 and the axis of ordinates showing the amount of transmission loss (dB).

[0047] As can be seen from Fig. 9 and Fig. 10, coupler 21 exhibits excellent reflection characteristics and transmission characteristics over a broad band.

[0048] Furthermore, the thickness of round insulation plates 21_{51} and 21_{52} of coupler 21 can be selected according to the transmission frequency band, and the bandwidth can be broadened by increasing the thickness from the selected thickness.

[0049] Fig. 11 shows observation results of changes in phase of the output from output terminal 24_1 of 90° 3-dB hybrid circuit 24 with respect to the phase of the input to input terminal 22_1 of 90° 3-dB hybrid circuit 22, the axis of abscissas showing the frequencies relative to the design frequency f_0 and the axis of ordinates showing the amount of phase shift ($^\circ$) with respect to the angle of rotation ϕ , each of the dimensions of coupler 21 being selected in the same way as explained for Fig. 9, the phase shifting device being configured with 90° 3-dB hybrid circuit 22 connected to coupler 21 by way of coaxial cables 26_1 and 26_2 and 90° 3-dB hybrid circuit 24 connected to coupler 21 by way of coaxial cables 27_1 and 27_2 as shown in Fig. 3, and ϕ representing the angle of rotation by which the sealed cases 21_1 and 21_2 forming coupler 21 have been rotated relative to each other around their common cylindrical axis.

[0050] As is clear from Fig. 11, regardless of the transmission frequency, the amount of phase shift always coincides with the angle of rotation ϕ of sealed cases 21_1 and 21_2 making up coupler 21 with respect to each other around their common cylindrical axis.

[0051] Fig. 12 shows the observation results of the amount of transmission loss between input terminal 22_1 of 90° 3-dB hybrid circuit 22 and output terminal 24_1 of 90° 3-dB hybrid circuit 24 under the same conditions as for the observations in which the results of Fig. 11 were obtained, the axis of abscissas being the same as for Fig. 11 and the axis of ordinates showing the amount of transmission loss (dB).

[0052] As is clear from Fig. 12, compared to the amount of transmission loss shown in Fig. 10 for coupler 21 alone, the addition of 90° 3-dB hybrid circuits 22 and 24, coaxial cables 26_1 and 26_2 , as well as 27_1 and 27_2 increases the transmission loss, but the degree of change in the frequency characteristic of the amount of transmission loss is as for coupler 21 alone.

[0053] The foregoing explanation relates to a case in which sealed cases 21_1 and 21_2 of coupler 21 are formed from metal; the first driver installed within coupler 21 is formed from a microstrip antenna composed of sealed case 21_1 , which is the ground conductor, round insulation plate 21_{51} , and driver element 21_{61} ; and the second driver is formed from a microstrip antenna composed of sealed case 21_2 , which is the ground conductor, round insulation plate 21_{52} , and driver element 21_{62} . However, in a case in which sealed cases 21_1 and 21_2 are formed by applying a metal film to the outer surface of a body composed of a suitable synthetic resin, the metal film applied to the outer surface of the body of sealed case 21_1 can serve as the ground conductor, the body of sealed case 21_1 can serve as round insulation plate 21_{51} , and the first driver composed of a microstrip antenna can therefore be formed by attaching driver element 21_{61} to the inner surface of the bottom wall of sealed case 21_1 , and the second driver composed of a microstrip antenna can similarly be formed by attaching driver element 21_{62} to the inner surface of the bottom wall of sealed case 21_2 .

[0054] In a case in which sealed cases 21_1 and 21_2 are formed by multilayer stacking of dielectric plates, the first driver composed of a microstrip antenna can be formed by attaching driver element 21_{61} to the inner surface of the bottom wall of sealed case 21_1 and attaching a ground conductor to the outer surface of the bottom wall; and the second driver composed of a microstrip antenna can be formed by attaching driver element 21_{62} to the inner surface of the bottom wall of sealed case 21_2 and attaching a ground conductor to the outer surface of the bottom wall.

[0055] Instead of forming the driver as a microstrip antenna, the driver can also be formed from a slot antenna formed by providing a cross-shaped slot 21_{71} in the central portion of metal plate or metal film 21_{61} forming the driver element as shown in Fig. 13, which is a sectional view taken along the same line as Fig. 6. Other construction and reference numerals in Fig. 13 are as for Fig. 6.

[0056] In Fig. 14, which is a sectional view taken along the same line as Fig. 7, 21_{71} is cross-shaped slot, and 21_{72} , like 21_{71} , is a cross-shaped slot provided in the central portion of the metal plate or metal film 21_{62} forming the driver element, the other construction and reference numerals being the same as for Fig. 7.

[0057] In this embodiment as well, if sealed cases 21_1 and 21_2 are formed by applying a metal film to the outer surface of a base body composed of a suitable synthetic resin, the metal film applied to the outer surface of the base body can serve as the ground conductor and the base body itself can be used as round insulation plates 21_{51} and 21_{52} of Fig. 14; and if sealed cases 21_1 and 21_2 are formed by multilayer stacking of dielectric plates, the first and second drivers composed of slot antennas can be formed by attaching driver elements 21_{61} and 21_{62} composed of metal films or metal plates provided with cross-shaped slots to the inner surface of each of the bottom walls of sealed cases 21_1 and 21_2 , and providing a ground conductor on the outer surface of each bottom wall.

[0058] Further, probes may be connected to internal conductors 21_{41} and 21_{42} of coaxial connection plugs 21_{31} and 21_{32} shown in Fig. 6 or Fig. 13, these probes being formed such that the longitudinal direction of both probes is parallel to metal plate or metal film 21_{61} , the portions of both probes extending in the longitudinal direction intersect at the center point of metal plate or metal film 21_{61} , and this intersecting angle is a right angle. A driver composed of probes similar to the sealed case 21_1 side may then be provided on the sealed case 21_2 side.

[0059] Whichever of the above constructions is adopted for the drivers installed in each of sealed cases 21_1 and 21_2 , the amount of phase shift between the input and output is determined by the angle of relative rotation between

sealed cases 21_1 and 21_2 , and in order for sealed cases 21_1 and 21_2 to rotate with respect to each other, any of the following constructions may be adopted: coaxial cables 26_1 , 26_2 , 27_1 , and 27_2 are formed as flexible cables; the sealed case 21_2 side is fixed and sealed case 21_1 , coaxial cables 26_1 and 26_2 , and 90° 3-dB hybrid circuit 22 rotate as a unit; the sealed case 21_1 side is fixed and sealed case 21_2 , coaxial cables 27_1 and 27_2 , and 90° 3-dB hybrid circuit 24 rotate as a unit; or sealed case 21_1 , coaxial cables 26_1 and 26_2 , and 90° 3-dB hybrid circuit 22 are formed as one rotatable unit and sealed case 21_2 , coaxial cables 27_1 and 27_2 and 90° 3-dB hybrid circuit 24 are formed as another rotatable unit.

[0060] The foregoing explanations relate to cases in which sealed cases 21_1 and 21_2 are each formed as a cylinder with one closed end, but either of sealed case 21_1 or 21_2 may be formed as a cylindrical case with one closed end in which is installed either the first or second driver, and the other side, i.e., sealed case 21_2 or 21_1 , may be formed as a disk-shaped cover with the second or first driver attached to the inner surface, this cover being formed to rotatably fit with the end portion of the opening of the closed cylinder body.

[0061] As is clear from the foregoing explanation, in this phase shifting device, the side of coaxial cables 26_1 and 26_2 and 90° 3-dB hybrid circuit 22 and the side of coaxial cables 27_1 and 27_2 and 90° 3-dB hybrid circuit 24 are formed symmetrically to each other across the plane cutting through the midsection of the coupler 21 at F-F in Fig. 15; and consequently, precisely identical operation can be achieved as explained in conjunction with Fig. 8 even if terminal 24_1 of 90° 3-dB hybrid circuit 24 is made the input terminal and terminal 22_1 of 90° 3-dB hybrid circuit 22 is made the output terminal. The other reference numerals of Fig. 15 are equivalent to those of Fig. 3.

[0062] The foregoing explanation relates to an example in which 90° 3-dB hybrid circuits 22 and 24 and reflectionless terminators 23 and 25 have been used for the two-partition circuit of the input and the combining circuit of the output, but for a case in which the transmission frequency bandwidth is relatively narrow, the input- and output-side 90° 3-dB hybrid circuits 22 and 24 and reflectionless terminators 23 and 25 can be replaced by two-branch terminal circuits, with one of coaxial cables 26_1 and 26_2 connecting coaxial connection plugs 21_{31} and 21_{32} of coupler 21 with the two output terminals of the two-branch terminal circuit on the input side, for example, coaxial cable 26_2 , being formed exactly one transmission quarter-wavelength longer than coaxial cable 26_1 , and one of coaxial cables 27_1 and 27_2 connecting coaxial connection plugs 21_{33} and 21_{34} of coupler 21 to the two input terminals of the two-branch terminal circuit on the output side, for example coaxial cable 27_1 , being formed exactly one transmission quarter-wavelength longer than coaxial cable 27_2 .

[0063] In this embodiment, although the lengths of coaxial cables 26_1 and 26_2 must be made to differ by exactly one transmission quarter-wavelength, and the lengths of coaxial cables 27_1 and 27_2 similarly must be made to differ by exactly one transmission quarter-wavelength, the difference in lengths for both sets of cables is fixed at one transmission quarter-wavelength, and fabrication is therefore relatively easy.

[0064] If the difference in lengths between coaxial cables 26_1 and 26_2 and the difference in lengths between coaxial cables 27_1 and 27_2 is selected to be one quarter-wavelength of the center frequency of the transmission band, the difference in length between the coaxial cables will not precisely match the quarter-wavelength for frequencies outside the center frequency, but since this embodiment is intended for applications in which the transmission frequency band is relatively narrow, any operational error arising due to variance from the quarter-wavelength is minute and presents no practical problem.

[0065] The foregoing explanation relates to a case in which the phase shifting device of the present invention is constructed by assembling three-dimensional constituent elements, but the entire structure can be miniaturized by forming 90° 3-dB hybrid circuits 22 and 24 and reflectionless terminators 23 and 25 on a printed circuit board using a printed wiring method, and forming coaxial cables 26_1 , 26_2 , 27_1 and 27_2 as microstrip wiring.

[0066] The entire structure may also be made extremely compact and concise by providing dielectric layers on the outer surfaces of sealed cases 21_1 and 21_2 of coupler 21, and then forming by a printed wiring method on the dielectric layer provided on the outer surface of sealed case 21_1 microstrip wiring that takes the place of 90° 3-dB hybrid circuit 22, reflectionless terminator 23 and coaxial cables 26_1 and 26_2 , and forming by a printed wiring method on the dielectric layer provided on the outer surface of sealed case 21_2 microstrip wiring that takes the place of 90° 3-dB hybrid circuit 24, reflectionless terminator 25 and coaxial cables 27_1 and 27_2 .

[0067] In a case in which two-branch terminal circuits are used in place of 90° 3-dB hybrid circuits 22 and 24 and reflectionless terminators 23 and 25, the entire structure can be miniaturized through formation on printed circuit boards or on dielectric layers provided on the outer surfaces of each of sealed cases 21_1 and 21_2 .

[0068] Fig. 16 presents a phase shifting device according to another embodiment of the present invention.

[0069] The phase shifting device of this embodiment is constructed from a coupler 31 composed of cylindrical sealed cases 31_1 and 31_2 having one closed end, and terminals 31_{31} - 31_{33} composed of, for example, coaxial connection plugs; 90° 3-dB hybrid circuit 32 composed of, for example, a quarter-wave coupled line-type directional coupler including input terminal 32_1 , isolation terminal 32_2 , and output terminals 32_3 and 32_4 ; coaxial cable 33_1 connecting terminal 31_{33} and input terminal 32_1 ; and coaxial cable 33_2 connecting terminal 31_{32} and isolation terminal 32_2 . Here, considering a signal inputted to input terminal 32_1 , the phase of the output from output terminal 32_3 is delayed substantially 90° with respect to the phase of the output of output terminal 32_4 . In addition, the length of each of coaxial

cable 33₁ and 33₂ is adjusted such that the phase difference between inputs at the input end of each of coaxial cables 33₁ and 33₂ is maintained unchanged when outputted from the output end of each of coaxial cables 33₁ and 33₂.

[0070] Fig. 17 shows a side view of coupler 31 of Fig. 16, and Fig. 18 shows a plan view of the sealed case 31₁ side of coupler 31 as seen from the side of the bottom wall, the reference numerals used in Figs. 17 and 18 being the same as those used in Fig. 16. Fig. 19 is an enlarged sectional view taken at line G-G of Fig. 16, Fig. 20 is an enlarged sectional view taken at line H-H of Fig. 17, and Fig. 21 is an enlarged sectional view taken at line I-I of Fig. 18.

[0071] As can be clearly seen from Fig. 21, stepped portions are formed in the side walls at the end portions of the openings of each of sealed cases 31₁ and 31₂, the end portion of the opening of one of the sealed cases, in this case sealed case 31₂, fitting inside the end portion of the opening of the other sealed case 31₁, the two sealed cases 31₁ and 31₂ being mechanically and electrically coupled, and sealed cases 31₁ and 31₂ able to rotate relative to each other around their cylindrical axis.

[0072] Sealed cases 31₁ and 31₂ are manufactured by machining a metal block or press-forming a metal sheet in the prescribed shape; by forming a suitable synthetic resin in a preliminary form of the prescribed shape and subsequently applying a metal film to the surface by an electroless plating or vacuum evaporation process; or by multilayer stacking of dielectric plates having an appropriate dielectric constant and forming as a cylinder with one closed end that shields electromagnetic energy in accordance with Snell's law.

[0073] Coaxial connection plugs 31₃₁ to 31₃₃ have internal conductors 31₄₁ to 31₄₃. Round insulation plates 31₅₁ and 31₅₂ are composed of a material having excellent highfrequency characteristics such as an organic material such as polyethylene or fluorinated ethylene or an inorganic material such as a ceramic and have a thickness less than the transmission wavelength, round insulation plate 31₅₁ being secured to the inner surface of the bottom wall of sealed case 31₁, round insulation plate 31₅₂ being secured to the inner surface of the bottom wall of sealed case 31₂, and each being secured using a suitable adhesive.

[0074] Metal plate 31₆₁ is secured to the surface of round insulation plate 31₅₁ using a suitable adhesive, and in addition, a portion of its periphery is electrically connected to internal conductor 31₄₁ of coaxial connection plug 31₃₁. First driver composed of a microstrip antenna is formed with sealed case 31₁ on the opposing side of insulation plate 31₅₁ serving as ground conductor, metal plate 31₆₁ serving as first driver element, and the connection point between internal conductor 31₄₁ of coaxial connection plug 31₃₁ and metal plate 31₆₁ serving as the driver point.

[0075] Metal plate 31₆₂ is secured to the surface of round insulation plate 31₅₂ using a suitable adhesive, and in addition, portions of its periphery are electrically connected to internal conductors 31₄₂ and 31₄₃ of coaxial connection plugs 31₃₂ and 31₃₃. Second driver composed of a microstrip antenna is formed with sealed case 31₂ on the opposing side of insulation plate 31₅₂ serving as ground conductor, metal plate 31₆₂ serving as second driver element, and the connection points between metal plate 31₆₂ and internal conductors 31₄₂ and 31₄₃ of coaxial connection plugs 31₃₂ and 31₃₃ serving as the driver points.

[0076] As can be seen from Fig. 20, a right angle is formed by the intersection of the straight line joining the center of metal plate 31₆₂ with the driving point composed of the connection point between internal conductor 31₄₂ of coaxial connection plug 31₃₂ and metal plate 31₆₂, and the straight line joining the center of metal plate 31₆₂ with the driving point formed by the connection point between internal conductor 31₄₃ of coaxial connection plug 31₃₃ and metal plate 31₆₂.

[0077] In addition, the spacing between first driver element 31₆₁ and second driver 31₆₂ is set at less than the transmission wavelength.

[0078] The external conductor of coaxial connection plug 31₃₁ is electrically connected to sealed case 31₁, and the external conductors of each of coaxial connection plugs 31₃₂ and 31₃₃ are connected to sealed case 31₂; but, as shown in Fig. 21, a gap is provided by removing a portion of the sealed case 31₁ in the vicinity of internal conductor 31₄₁ and a gap is provided by removing a portion of sealed case 31₂ in the vicinity of internal conductor 31₄₃ such that internal conductors 31₄₁ and 31₄₃ of coaxial connection plugs 31₃₁ and 31₃₃ do not mechanically contact sealed cases 31₁ and 31₂. Although not shown in Fig 21, a gap is similarly provided in sealed case 31₂ in the vicinity of internal conductor 31₄₂ of coaxial connection plug 31₃₂.

[0079] Rather than using an adhesive as a means of securing metal plate 31₆₁ or 31₆₂ to the surface of round insulation plate 31₅₁ or 31₅₂, the center of metal plate 31₆₁ or 31₆₂ (the portion where electric field intensity is 0) may be secured to round insulation plate 31₅₁ or 31₅₂ using a setscrew, or alternatively the center of metal plate 31₆₁ or 31₆₂ may be screwed to the bottom wall of sealed case 31₁ or 31₂ through round insulation plate 31₅₁ or 31₅₂.

[0080] Rather than forming the driver element of the microstrip antenna constituting the first or second driver from metal plate 31₆₁ or 31₆₂, the driver element may be formed by applying a metal film to the surface of round insulation plate 31₅₁ or 31₅₂ using a vacuum evaporation process and finishing to the required outline shape by a process such as etching.

[0081] Whether the driver element is formed from a metal plate or metal film, its outline shape may be formed as a square instead of the circle shown in Fig. 19 and Fig. 20.

[0082] Regarding the dimensions of driver elements 31₆₁ and 31₆₂ for cases in which driver elements 31₆₁ and 31₆₂

are driven in basic mode, if the outline shape of these elements is formed as a circle, the specific inductive capacity of round insulation plates 31₅₁ and 31₅₂ is ϵ_r and the design frequency is f_0 , the radius of driver elements 31₆₁ and 31₆₂ is preferably selected to be substantially $1.841 C/(2\pi \cdot f_0 \cdot \epsilon_r^{1/2})$; and if the outline shape of driver elements 31₆₁ and 31₆₂ is formed as a square, the length of one side is preferably selected to be substantially $C/(2f_0 \cdot \epsilon_r^{1/2})$ (where C is the speed of light).

[0083] Fig. 22 illustrates the operation of the present phase shifting device.

[0084] The input applied to coaxial connection plug 31₃₁ of coupler 31 passes through internal conductor 31₄₁ and drives driver element 31₆₁ in the first driver.

[0085] If the X-axis and Y-axis are established as shown in Fig. 19, Fig. 20, and Fig. 22A, electric field vector E produced by driver element 31₆₁ driven as described above can be divided between two orthogonal components E_X and E_Y as shown in Fig. 22A. These couple at driver element 31₆₂ of the second driver in the form:

$$E = E_X + E_Y = E \cos \phi + \sin \phi$$

[0086] As described hereinabove, this device is formed such that a right angle is formed by the intersection of the straight line joining the center of driver element 31₆₂ with the driving point constituted by the connection point between driver element 31₆₂ and internal conductor 31₄₂ of coaxial connection plug 31₃₂ and the straight line joining the center of driver element 31₆₂ with the driving point constituted by the connection point between driver element 31₆₂ and internal element 31₄₃ of coaxial connection plug 31₃₃; and therefore, when driver element 31₆₂ is driven in basic mode, coupling between coaxial connection plugs 31₃₂ and 31₃₃ becomes sparse and quadrature mode coupling is enabled.

[0087] The quadrature mode coupling to driver element 31₆₂ causes component E_X to be outputted from coaxial connection plug 31₃₂ and component E_Y to be outputted from coaxial connection plug 31₃₃, the two outputs being respectively inputted to terminals 32₁ and 32₂ of 90° 3-dB hybrid circuit 32 by way of coaxial cables 33₁ and 33₂.

[0088] If the output of output terminals 32₄ and 32₃ of 90° 3-dB hybrid circuit 32 are E_1 and E_2 , respectively:

$$\begin{aligned} E_1 &= \frac{E}{\sqrt{2}} \sin \phi - j \frac{E}{\sqrt{2}} \cos \phi \\ &= \frac{E}{\sqrt{2}} e^{-j\{(\pi/2)-\phi\}} \end{aligned}$$

$$E_2 = \frac{E}{\sqrt{2}} \cos \phi - j \frac{E}{\sqrt{2}} \sin \phi = \frac{E}{\sqrt{2}} e^{-j\pi}$$

[0089] Although the phase of output E_1 shifts in a counterclockwise direction with increase in declination angle ϕ of electric field vector E from the X-axis as shown in Fig. 22A, the amplitude remains unchanged. The phase of output E_2 also shifts in a clockwise direction with increase in declination angle ϕ of electric field vector E from the X-axis, but again, the amplitude remains unchanged. Accordingly, if the declination angle ϕ of electric field vector E from the X-axis is 45° or 225°, the amplitude as well as the phase of both outputs E_1 and E_2 are equal, but if the declination angle ϕ increases from 45° or 225°, the phase of output E_1 shifts in the advance direction, and the phase of output E_2 shifts in the delay direction. If the declination angle ϕ of electric field vector E from the X-axis further increases to 135° or 315°, the phase relation between outputs E_1 and E_2 is mutually reversed.

[0090] Fig. 23 shows the reflection characteristic at coaxial connection plug 31₃₁ observed after removing coaxial cables 33₁ and 33₂ from coaxial connection plugs 31₃₂ and 31₃₃, the inner diameter of the cylinders with one closed end forming sealed cases 31₁ and 31₂ of coupler 31 being selected as $0.285 \lambda_0$ (λ_0 being the free-space wavelength corresponding to the design frequency f_0), the distance of opposition between the bottom wall of sealed case 31₁ and the bottom wall of sealed case 31₂ as $0.089 \lambda_0$, the specific inductive capacity of round insulation plates 31₅₁ and 31₅₂ as 10, the dielectric dissipation factor of each of round insulation plates 31₅₁ and 31₅₂ as 0.0055, the thickness of each of round insulation plates 31₅₁ and 31₅₂ as $0.023 \lambda_0$, the outline shape of first and second driver elements 31₆₁ and 31₆₂ being formed as a circle with a diameter of $0.21 \lambda_0$, the axis of abscissas in the figure being the relative frequency for the design frequency f_0 , and the axis of ordinates being the amount of return loss (dB). Fig. 24 shows the transmission characteristics between coaxial connection plugs 31₃₁ and 31₃₃ observed with coaxial cable 33₁ and 33₂ removed from coaxial connection plugs 31₃₂ and 31₃₃ and the selected values of the dimensions of each of the parts of coupler 31 being the same as described for Fig. 23, the horizontal axis of the figure being the same as for Fig. 23 and the vertical axis being the amount of transmission loss (dB).

[0091] As is clear from Fig. 23 and Fig. 24, coupler 31 exhibits excellent reflection characteristics and transmission characteristics across a broad band.

[0092] In addition, the thickness of round insulation plates 31_{51} and 31_{52} in coupler 31 can be selected according to the transmission frequency band, and the bandwidth can be broadened by increasing the selected thickness.

[0093] Fig. 25 shows the results of observing the phase shift of output E_1 of coaxial connection plug 31_{33} and output E_2 of coaxial connection plug 31_{32} upon change of declination angle ϕ to 90° or 135° with 45° as a standard. Here, the same values are selected for the dimensions of each part of coupler 31 as described for Fig. 23; the phase shifting device is configured as shown in Fig. 16, wherein 90° 3-dB hybrid circuit 32 is connected to coupler 31 by way of coaxial cables 33_1 and 33_2 ; and sealed cases 31_1 and 31_2 , which make up coupler 31, are rotated relative to each other around their common cylindrical axis. The angle of declination ϕ is formed by the straight line joining the center of driver element 31_{62} with the connection point between internal conductor 31_{42} of coaxial connection plug 31_{32} and driver element 31_{62} in the second driver installed on the sealed case 31_2 side, i.e., the X-axis, and the electric field vector E arising due to drive of driver element 31_{61} in the first driver installed on the sealed case 31_1 side. For both outputs E_1 and E_2 , the absolute value of the change in phase and the change in declination angle ϕ match without any dependence on transmission frequency, and the code of phase of outputs E_1 and E_2 differ. Accordingly, the phase difference between outputs E_1 and E_2 with respect to change in declination angle ϕ is 2ϕ .

[0094] The axis of abscissas of Fig. 25 is the same as for Fig. 23, and the axis of ordinates shows declination angle ϕ , i.e., the amount of phase shift ($\cdot$) with respect to the relative angle of rotation ϕ between sealed cases 31_1 and 31_2 .

[0095] Fig. 26 shows the amount of transmission loss between coaxial connection plug 31_{31} of coupler 31 and output terminal 32_3 of 90° 3-dB hybrid circuit 32, and between coaxial connection plug 31_{31} of coupler 31 and output terminal 32_4 of 90° 3-dB hybrid circuit 32, the observation results being obtained under the same conditions as those for Fig. 25, the axis of abscissas being the same as Fig. 25 and the axis of ordinates showing the amount of transmission loss (dB).

[0096] As is clear from Fig. 26, although the addition of 90° 3-dB hybrid circuit 32 and coaxial cables 33_1 and 33_2 results in increased transmission loss as compared with the amount of transmission loss for the case shown in Fig. 24 in which coupler 31 alone is used, the differences in the change of phase shift of outputs E_1 and E_2 with respect to the change in angle ϕ or in amplitude of outputs E_1 and E_2 are virtually negligible.

[0097] Fig. 27 shows an example which employs both outputs E_2 and E_1 of output terminals 32_3 and 32_4 of 90° 3-dB hybrid circuit 32. Reference numeral 34 indicates the phase shifting device shown in Fig. 16, 31_{31} is the input terminal of coupler 31 in phase shifting device 34, 32_3 and 32_4 are the output terminals of 90° 3-dB hybrid circuit 32 in phase shifting device 34, and 35_1 and 35_2 are both subarray antennas composed of a plurality of element antennas.

[0098] The locus joining the peaks of each of output vectors E_X and E_Y corresponding to the change in the relative angle of rotation ϕ between sealed cases 31_1 and 31_2 which make up coupler 31 in phase shifting device 34 is an oval, but the angle at which output vectors E_X and E_Y begin to describe an oval both differs by 90° and is in the opposite direction of rotation, and consequently, the phase difference between outputs E_2 and E_1 can be freely selected. Accordingly, the direction of maximum radiation and the side-lobe characteristics of the array antenna composed of subarray antennas 35_1 and 35_2 can be controlled by supplying outputs E_2 and E_1 of output terminals 32_3 and 32_4 as the driving power of subarray antennas 35_1 and 35_2 .

[0099] A comparison of Fig. 27 and Fig. 2 clearly shows that, while the structure of a power supply circuit using a phase shifting device of the prior art was complicated by the requirement for a transmission path having a standard amount of phase shift and a two-branch circuit for each phase shifter, the use of a phase shifting device of the present invention results in a power supply circuit of extremely simple construction because the phase shifting device of the present invention has an effect equivalent to the combination of a prior-art phase shifting device, a transmission path having a standard amount of phase shift, and a two-branch circuit.

[0100] The foregoing description relates to an example in which sealed cases 31_1 and 31_2 of coupler 31 are formed from metal; the first driver installed in coupler 31 is formed from a microstrip antenna composed of sealed case 31_1 which serves as a ground conductor, round insulation plate 31_{51} , and driver element 31_{61} ; and the second driver is formed from a microstrip antenna composed of sealed case 31_2 which serves as a ground conductor, round insulation plate 31_{52} , and driver element 31_{62} . However, if sealed cases 31_1 and 31_2 are each formed by applying a metal film to the outer surface of a base body composed of a suitable synthetic resin, the metal film applied to the outer surface of the base body of sealed case 31_1 can be used as a ground conductor, the base body itself of sealed case 31_1 can be used as round insulation plate 31_{51} , and as a result, the first driver composed of a microstrip antenna can be formed by attaching driver element 31_{61} to the inner surface of the bottom wall of sealed case 31_1 , and the second driver composed of a microstrip antenna can be formed by attaching driver element 31_{62} to the inner surface of the bottom wall of sealed case 31_2 .

[0101] For a case in which sealed cases 31_1 and 31_2 are formed by multilayer stacking of dielectric plates, the first driver composed of a microstrip antenna can be formed by attaching driver element 31_{61} to the inner surface and attaching a ground conductor to the outer surface of the bottom wall of sealed case 31_1 , and the second driver composed

of a microstrip antenna can be formed by attaching driver element 31₆₂ to the inner surface and attaching a ground conductor to the outer surface of the bottom wall of sealed case 31₂.

[0102] As shown in Fig. 28 in a sectional view similar to that of Fig. 20, instead of being formed from a microstrip antenna, the second driver may be formed from a slot antenna achieved by providing a cross-shaped slot 31₇ in the center of metal plate or metal film 31₆₂ forming the driver element; and the first driver may be formed as a slot antenna composed of only a slot in the vertical direction or in the horizontal direction of the cross-shaped slot of Fig. 28. Other reference numerals and construction in Fig. 28 is as for Fig. 20.

[0103] In this embodiment as well, if sealed cases 31₁ and 31₂ are formed by applying a metal film to the outer surface of a base body composed of a suitable synthetic resin, the metal film applied to the outer surface of the base body may be used as the ground conductor, and the base body itself can be used as round insulation plates 31₅₁ and 31₅₂; and if sealed cases 31₁ and 31₂ are formed by multilayer stacking of dielectric plates, first and second drivers composed of slot antennas can be formed by attaching driver elements 31₆₁ and 31₆₂ composed of a metal plate or metal film provided with a single-line slot or a cross-shaped slot to the inner surfaces of the bottom walls of each of sealed cases 31₁ and 31₂ and attaching ground conductors to the outer surfaces of each bottom wall.

[0104] In addition, the first driver may be formed by connecting a probe to internal conductor 31₄₁ of coaxial connection plug 31₃₁ shown in Fig. 19; and the second driver may be formed by connecting probes to internal conductors 31₄₂ and 31₄₃ of coaxial connection plug 31₃₂ and 31₃₃ shown in Fig. 20, the longitudinal direction of both probes being parallel to metal plate or metal film 31₆₂ and the portions extending in the longitudinal direction of both probes intersecting at the center point of metal plate or metal film 31₆₂, this intersection being a right angle.

[0105] In either of the above-described constructions of the first and second drivers installed in sealed cases 31₁ and 31₂, respectively, the amount of phase shift between input and output is determined according to the relative angle of rotation between sealed cases 31₁ and 31₂, and to rotate sealed cases 31₁ and 31₂ relative to each other, a construction may be adopted wherein sealed case 31₂, coaxial cables 33₁ and 33₂, and 90° 3-dB hybrid circuit 32 are fixed and sealed case 31₁ is caused to rotate; wherein sealed case 31₁ is fixed and sealed case 31₂, coaxial cables 33₁ and 33₂, and 90° 3-dB hybrid circuit 32 are caused to rotate as a unit; or wherein sealed case 31₁ and 90° 3-dB hybrid circuit 32 are fixed, coaxial cables 33₁ and 33₂ is formed from a flexible cable, and sealed case 31₂ is caused to rotate.

[0106] The foregoing explanation relates to a case in which sealed cases 31₁ and 31₂ are both formed as cylinders with one closed end, but either sealed case 31₁ or 31₂ may be formed as a cylinder with one closed end in which the first or second driver is installed, and the other sealed case, i.e., sealed case 31₂ or 31₁ may be formed as a disk-shaped cover with the second or first driver attached to its inner surface and formed such that the cover rotatably fits with the end portion of the opening of the cylinder with one closed end.

[0107] The foregoing explanation relates to a case in which 90° 3-dB hybrid circuit 32 is formed as a quarter-wave coupled-line directional coupler, but the hybrid circuit may also be formed as a branch line directional coupler.

[0108] In addition, for cases in which the transmission frequency bandwidth is relatively narrow, a two-branch terminal circuit may take the place of 90° 3-dB hybrid circuit 32, and the length of one of coaxial cables 33₁ and 33₂, for example coaxial cable 33₂, may be formed exactly one transmission quarter-wavelength longer than coaxial cable 33₁.

[0109] In this embodiment, the lengths of coaxial cable 33₁ and 33₂ must differ by exactly one transmission quarter-wavelength, but fabrication is relatively easy because the difference in length between coaxial cables 33₁ and 33₂ is fixed at one transmission quarter-wavelength.

[0110] If the difference in lengths between coaxial cables 33₁ and 33₂ is selected to be one transmission quarter-wavelength for the center frequency of the transmission band, the difference in length between the coaxial cables will not precisely match the quarter-wavelength for frequencies outside the center frequency, but since this embodiment is intended for applications in which the transmission frequency band is relatively narrow, any operational error arising due to variance from the quarter-wavelength is minute and presents no practical problem.

[0111] The foregoing explanation relates to a case in which the phase shifting device is constructed by assembling three-dimensional constituent elements, but the entire structure can be miniaturized by forming 90° 3-dB hybrid circuit 32 on a printed circuit board using a printed wiring method and forming coaxial cables 33₁ and 33₂ as microstrip wiring.

[0112] The entire structure may also be made extremely compact and concise by providing a dielectric layer on the outer surface of sealed case 31₂ of coupler 31, and then employing a printed wiring method to form 90° 3-dB hybrid circuit 32 and microstrip wiring that takes the place of coaxial cables 33₁ and 33₂.

[0113] In a case in which a two-branch terminal circuit takes the place of 90° 3-dB hybrid circuit 32, the entire structure can be miniaturized by forming this component on a printed circuit board or on a dielectric layer provided on the outer surface of sealed cases 31₂.

Claims

1. A phase shifting device comprising:

two-partition circuit means (22) for partitioning input power into two substantially equal portions having a mutual phase difference of substantially 90° ;
 a first microwave antenna means (21_{61}) driven by two-partitioned output of said two-partition circuit means for generating circularly polarized waves and a second microwave antenna means (21_{62}) for coupling circularly polarized waves generated by said first microwave antenna means, said first and second antenna means are installed as to be rotatable relative to each other around the axis joining the centers of both antennae; and a combining circuit means (24,27) for combining two outputs generated from circularly polarized waves coupled in said second microwave antenna means;

characterized in,

that an electrically conductive enclosure ($21_1, 21_2$) is provided within which said first and second microwave antenna means ($21_{61}, 21_{62}$) are installed, and having an inside diameter substantially equal to $0,285 \lambda_0$, where λ_0 is the free space wavelength corresponding to the designed frequency f_0 .

2. A phase shifting device according to claim 1, wherein the electrically conductive enclosure ($21_1, 21_2$) comprises first and second cylinders, each having one closed end for installing said first and second microwave antenna means ($21_{61}, 21_{62}$) therein, the end portion of the opening of said first cylinder fitting with the end portion of the opening of said second cylinder, said first and second cylinders being rotatable to each other about their cylindrical axis.

3. A phase shifting device according to claim 1, wherein the electrically conductive enclosure (21_1 or 21_2) comprises a cylinder with one closed end for installing therein either one of said first and second microwave antenna means ($21_{61}, 21_{62}$) and a disk-shaped cover which fits with the end portion of the opening of said cylinder and upon the inner surface of which is attached the other of said first and second microwave antenna means, said cylinder and said cover being rotatable relative to each other about the cylindrical axis of said cylinder.

4. A phase device according to one of claims 1 to 3, wherein said first and second microwave antenna means each comprise microstrip antennae ($21_{61}, 21_{62}$).

5. A phase shifting device according to one of claims 1 to 3, wherein said first and second microwave antenna means each comprises slot antennae (21_{71}).

6. A phase shifting device according to one of claims 1 to 3, wherein said first and second microwave antenna means ($21_{61}, 21_{62}$) each comprise two probes provided in the same plane in an orthogonal relationship.

7. A phase shifting device comprising:

a first microwave antenna means (31_{61}) driven by input applied by way of an input terminal (31_{31}) for generating linearly polarized waves and a second microwave antenna means (31_{62}) for coupling two orthogonal components of linearly polarized waves generated by said first microwave antenna means, said first and second antenna means are installed as to be rotatable relative to each other around the axis joining the centers of both antennae; and a combining circuit means (32,33) for combining two outputs generated from two orthogonal components of linearly polarized waves coupled in said second microwave antenna means,

characterized in,

that an electrically conductive enclosure ($31_1, 31_2$) is provided within which said first and second microwave antenna means ($31_{61}, 31_{62}$) are installed, and having an inside diameter substantially equal to $0,285 \lambda_0$, where λ_0 is the free space wavelength corresponding to the designed frequency f_0 .

8. A phase shifting device according to claim 7, wherein the electrically conductive enclosure ($31_1, 31_2$) comprises first and second cylinders, each having one closed end for installing said first and second microwave antenna means ($31_{61}, 31_{62}$) therein, the end portion of the opening of said first cylinder fitting with the end portion of the opening of said second cylinder, said first and second cylinders being rotatable to each other about their cylindrical axis.

9. A phase shifting device according to claim 7, wherein the electrically conductive enclosure (31₁ or 31₂) comprises a cylinder with one closed end for installing therein either one of said first and second microwave antenna means (31₆₁, 31₆₂) and a disk-shaped cover which fits with the end portion of the opening of said cylinder and upon the inner surface of which is attached the other of said first and second microwave antenna means, said cylinder and said cover being rotatable relative to each other about the cylindrical axis of said cylinder.
10. A phase shifting device according to one of claims 7 to 9, wherein said first and second microwave antenna means each comprise microstrip antennas (31₆₁; 31₆₂).
11. A phase shifting device according to one of claims 7 to 9, wherein said first and second microwave antenna means (31₆₁, 31₆₂) each comprise slot antennas.
12. A phase shifting device according to one of claims 7 to 9, wherein first microwave antenna means (31₆₁) comprises one probe, and said second microwave antenna means (31₆₂) comprise two probes provided in the same plane, extending portions of which are in an orthogonal relationship.
13. A phase shifting device according to one of claims 7 to 9, wherein said combining circuit means (32, 33) comprises a 90° 3-dB hybrid circuit (32).
14. A phase shifting device according to one of claims 7 to 9, wherein said combining circuit means (32) comprises a two-branch terminal circuit.

Patentansprüche

1. Phasenverschiebeanordnung, umfassend:

eine zweigeteilte Schaltkreisvorrichtung (22) zur Unterteilung der Eingabeenergie in zwei im wesentlichen gleiche Teile mit einer gegenseitigen Phasendifferenz von im wesentlichen 90°; eine erste Mikrowellen-Antennenvorrichtung 21, 21₆₁, die durch eine zweigeteilte Abgabe der zweigeteilten Schaltkreisvorrichtung zur Erzeugung zirkular polarisierter Wellen und eine zweite Mikrowellen-Antennenvorrichtung (21, 21₆₂) zum Kopplern zirkular polarisierter Wellen, die durch diese erste Mikrowellen-Antennenvorrichtung erzeugt werden, betrieben wird, wobei die erste und zweite Antennenvorrichtung gegeneinander drehbar um die Achse angeordnet sind, welche die Mittelpunkte der beiden Antennen verbindet; und eine Kombination der Schaltkreisvorrichtungen (24, 27) zur Kombination der beiden Abgaben, welche von den, in der zweiten Mikrowellen-Antennenvorrichtung gekoppelten zirkular polarisierten Wellen erzeugt werden;

dadurch gekennzeichnet,

dass ein elektrisch leitfähiges Gehäuse (21₁, 21₂) bereitgestellt ist, in dem die erste und zweite Mikrowellen-Antennenvorrichtung (21₆₁, 21₆₂) angebracht sind, und das einen Innendurchmesser besitzt, der im wesentlichen $0,285 \lambda_0$ ist, wobei λ_0 die der Bestimmungsfrequenz f_0 entsprechende Wellenlänge im leeren Raum ist.

2. Phasenschieberanordnung gemäß Anspruch 1, bei der das elektrisch leitfähige Gehäuse (21₁, 21₂) einen ersten und einen zweiten Zylinder umfasst, von denen jeder ein verschlossenes Ende zum Anbringen der ersten und zweiten Mikrowellen-Antennenvorrichtung (21₆₁, 21₆₂) hierin aufweist, wobei der Endteil der Öffnung des ersten Zylinders in den Endteil der Öffnung des zweiten Zylinders passt, und der erste und zweite Zylinder um ihre Zylinderachse gegenseitig drehbar sind.
3. Phasenschieberanordnung gemäß Anspruch 1, bei der das elektrisch leitfähige Gehäuse (21₁) oder (21₂) einen Zylinder mit einem geschlossenen Ende umfasst, um hierin eine der beiden ersten und zweiten Mikrowellen-Antennenvorrichtungen (21₆₁, 21₆₂) einzubauen, sowie einen scheibenförmigen Deckel, der in den Endteil der Öffnung des Zylinders passt, und auf dessen Innenfläche die andere der ersten und zweiten Mikrowellen-Antennenvorrichtung angebracht ist, wobei der Zylinder und der Deckel gegenseitig um die Zylinderachse des Zylinders drehbar sind.
4. Phasenschiebervorrichtung gemäß einem der Ansprüche 1 bis 3, bei der die erste und zweite Mikrowellen-Antennenvorrichtung jeweils eine Platinen-Antenne (21₆₁, 21₆₂) umfassen.

5. Phasenschieberanordnung gemäß einem der Ansprüche 1 bis 3, bei der die erste und zweite Mikrowellen-Antennenvorrichtung jeweils eine Schlitzantenne (21₇₁) umfasst.

6. Phasenschieberanordnung gemäß einem der Ansprüche 1 bis 3, bei der die erste und zweite Mikrowellen-Antennenvorrichtung (21₆₁, 21₆₂) jeweils 2, in der gleichen Ebene im orthogonalen Verhältnis bereitgestellte Sonden umfasst.

7. Phasenschieberanordnung, umfassend:

eine erste Mikrowellen-Antennenvorrichtung (31₆₁), die durch die Eingabe betrieben wird, welche über einen Eingabeanschluss (31₃₁) zugeführt wird, zur Erzeugung linear polarisierter Wellen, und eine zweite Mikrowellen-Antennenvorrichtung (31₆₂) zum Ankoppeln zweier orthogonaler Komponenten der durch die erste Mikrowellen-Antennenvorrichtung erzeugten linear polarisierten Wellen, wobei die erste und zweite Antennenvorrichtung so angebracht sind, dass sie gegenseitig um die Achse drehbar sind, welche die Mittelpunkte beider Antennen verbindet; sowie eine Kombinationsschaltung (32, 33) zum Vereinen zweier von den beiden orthogonalen Komponenten der linear polarisierten, in der zweiten Mikrowellen-Antennenvorrichtung gekoppelten Wellen erzeugter Abgaben,

dadurch gekennzeichnet,

dass ein elektrisch leitfähiges Gehäuse (31₁, 31₂) bereitgestellt ist, in dem die erste und zweite Mikrowellen-Antennenvorrichtung (31₆₁, 31₆₂) eingebaut sind, und die einen Innendurchmesser aufweisen, der im wesentlichen $0,285 \lambda_0$ gleich ist, wobei λ_0 die der Bestimmungsfrequenz f_0 entsprechende Wellenlänge im leeren Raum ist.

8. Phasenschieberanordnung gemäß Anspruch 7, bei der das elektrisch leitfähige Gehäuse (31₁, 31₂) einen ersten und zweiten Zylinder umfasst, der jeweils ein geschlossenes Ende zum Einbau der ersten und zweiten Mikrowellen-Antennenvorrichtung (31₆₁, 31₆₂) besitzt, wobei der Endteil der Öffnung des ersten Zylinders in den Endteil der Öffnung des zweiten Zylinders passt, und der erste und zweite Zylinder gegenseitig um ihre Zylinderachse drehbar sind.

9. Phasenschieberanordnung gemäß Anspruch 7, bei der das elektrisch leitfähige Gehäuse (31₁ oder 31₂) einen Zylinder mit einem geschlossenen Ende zum Einbau einer der beiden ersten und zweiten Mikrowellen-Antennenvorrichtungen (31₆₁, 31₆₂) und einen scheibenförmigen Deckel umfasst, der in den Endteil der Öffnung des Zylinders passt, und auf dessen Innenfläche die andere der ersten und zweiten Mikrowellen-Antennenvorrichtung angebracht ist, wobei der Zylinder und der Deckel gegenseitig um die Zylinderachse des Zylinders drehbar sind.

10. Phasenschieberanordnung gemäß einem der Ansprüche 7 bis 9, bei der die erste und zweite Mikrowellen-Antennenvorrichtung jeweils Platinen-Antennen (31₆₁, 31₆₂) umfasst.

11. Phasenschieberanordnung gemäß einem der Ansprüche 7 bis 9, bei der die erste und zweite Mikrowellen-Antennenvorrichtung (31₆₁, 31₆₂) jeweils Schlitzantennen umfasst.

12. Phasenschieberanordnung gemäß einem der Ansprüche 1 bis 9, bei der die erste Mikrowellen-Antennenvorrichtung (31₆₁) eine Sonde umfasst, und die zweite Mikrowellen-Antennenvorrichtung (31₆₂) zwei Sonden umfasst, welche in der gleichen Ebene vorgesehen sind, deren sich erstreckende Teile in einem orthogonalen Verhältnis stehen.

13. Phasenschieberanordnung gemäß einem der Ansprüche 7 bis 9, bei der die Kombinationsschaltung (32, 33) eine 90° 3dB Hybridschaltung (32) umfasst.

14. Phasenschieberanordnung gemäß einem der Ansprüche 7 bis 9, bei der die Kombinationsschaltung (32) eine Endschaltung mit zwei Verzweigungen umfasst.

Revendications

1. Dispositif de décalage de phase comprenant :

un moyen de circuit de partition en deux (22) pour partitionner la puissance d'entrée en deux parties substan-

tiellement égales ayant une différence de phase mutuelle substantiellement de 90° ;

un premier moyen d'antenne hyperfréquence (21, 21₆₁) commandé par une sortie partitionnée en deux dudit moyen de circuit de partition en deux pour générer des ondes polarisées circulairement et un second moyen d'antenne hyperfréquence (21, 21₆₂) pour coupler des ondes polarisées circulairement générées par ledit premier moyen d'antenne hyperfréquence (21, 21₆₁), lesdits premier et second moyens d'antenne sont installés pour pouvoir être mis en rotation l'un par rapport à l'autre autour d'un axe joignant les centres des deux antennes ; et un moyen de circuit de mélange (24, 27) pour mélanger les deux sorties générées à partir des ondes polarisées circulairement couplées dans ledit second moyen d'antenne hyperfréquence ;

caractérisé en ce que,

une enceinte conductrice électriquement (21₁, 21₂) est fournie à l'intérieur de laquelle sont installés lesdits premier et second moyens d'antenne hyperfréquence (21₆₁, 21₆₂), et ayant un diamètre interne substantiellement égal à $0,285 \lambda_0$, où λ_0 est une longueur d'onde d'espace libre correspondant à la fréquence désignée f_0 .

2. Dispositif de décalage de phase selon la revendication 1, dans lequel ladite enceinte conductrice électriquement (21₁, 21₂) comprend des premier et second cylindres, ayant chacun une extrémité fermée pour y installer lesdits premier et second moyens d'antenne hyperfréquence (21₆₁, 21₆₂) dans celle-ci, la partie d'extrémité d'ouverture dudit premier cylindre s'adaptant à la partie d'extrémité de l'ouverture dudit second cylindre, lesdits premier et second cylindres pouvant être mis en rotation l'un par rapport à l'autre autour de leur axe cylindrique.

3. Dispositif de décalage de phase selon la revendication 1, dans lequel ladite enceinte conductrice électriquement (21₁, 21₂) comprend un cylindre avec une extrémité fermée pour y installer soit l'un soit l'autre desdits premier et second moyens d'antenne hyperfréquence (21₆₁, 21₆₂) et un couvercle en forme de disque qui s'adapte à la partie d'extrémité de l'ouverture dudit cylindre et sur la surface interne duquel est fixée l'autre desdits premier et second moyens d'antenne hyperfréquence, ledit cylindre et ledit couvercle pouvant être mis en rotation l'un par rapport à l'autre autour de l'axe cylindrique dudit cylindre.

4. Dispositif de phase selon l'une des revendications 1 à 3, dans lequel lesdits premier et second moyens d'antenne hyperfréquence (21₆₁, 21₆₂) comprennent chacun des antennes microbande (21₆₁, 21₆₂).

5. Dispositif de décalage de phase selon l'une quelconque des revendications 1 à 3, dans lequel lesdits premier et second moyens d'antenne hyperfréquence comprennent chacun des fentes rayonnantes (21₇₁).

6. Dispositif de décalage de phase selon l'une des revendications 1 à 3, dans lequel lesdits premier et second moyens d'antenne hyperfréquence (21₆₁, 21₆₂) comprennent chacun deux sondes placées dans le même plan dans une relation orthogonale.

7. Dispositif de décalage de phase comprenant :

un premier moyen d'antenne hyperfréquence (31₆₁) commandé par une entrée appliquée au moyen d'une borne d'entrée (31₃₁) pour générer des ondes polarisées linéairement et un second moyen d'antenne hyperfréquence (31₆₂) pour coupler deux composantes orthogonales des ondes polarisées linéairement générées par ledit premier moyen d'antenne hyperfréquence, lesdits premier et second moyens d'antenne sont installés afin de pouvoir tourner l'un par rapport à l'autre autour d'un axe joignant les centres des deux antennes ; et un moyen de circuit de mélange (32, 33) pour mélanger deux sorties générées par deux composantes orthogonales des ondes polarisées linéairement couplées dans ledit second moyen d'antenne hyperfréquence ,

caractérisé en ce que

une enceinte conductrice électriquement (31₁, 31₂) est fournie à l'intérieur de laquelle sont installés lesdits premier et second moyens d'antenne hyperfréquence (31₆₁, 31₆₂) et ayant un diamètre interne substantiellement égal à $0,285 \lambda_0$, où λ_0 est la longueur d'onde d'espace libre correspondant à la fréquence désignée f_0 .

8. Dispositif de décalage de phase selon la revendication 7, dans lequel l'enceinte conductrice électriquement (31₁, 31₂) comprend des premier et second cylindres, chacun ayant une extrémité fermée pour y installer lesdits premier et second moyens d'antenne hyperfréquence (31₆₁, 31₆₂), la partie d'extrémité de l'ouverture dudit premier cylindre s'adaptant à la partie d'extrémité de l'ouverture du second cylindre, lesdits premier et second cylindres pouvant tourner l'un par rapport à l'autre autour de leur axe cylindrique.

9. Dispositif de décalage de phase selon la revendication 7, dans lequel l'enceinte conductrice électriquement (31₁, 31₂) comprend un cylindre avec une extrémité fermée pour y installer l'un ou l'autre desdits premier et second moyens d'antenne hyperfréquence (31₆₁, 31₆₂), et un couvercle en forme de disque qui s'adapte à la partie de l'extrémité d'ouverture dudit cylindre et sur la surface interne duquel est fixé l'autre desdits premier et second moyens d'antenne hyperfréquence, ledit cylindre et ledit couvercle pouvant tourner l'un par rapport à l'autre autour de l'axe cylindrique dudit cylindre.
10. Dispositif de décalage de phase selon l'une des revendications 7 à 9, dans lequel lesdits premier et second moyens d'antenne hyperfréquence comprennent chacun des antennes microbande (31₆₁, 31₆₂).
11. Dispositif de décalage de phase selon l'une des revendications 7 à 9, dans lequel lesdits premier et second moyens d'antenne hyperfréquence (31₆₁, 31₆₂) comprennent chacun des fentes rayonnantes.
12. Dispositif de décalage de phase selon l'une des revendications 7 à 9, dans lequel ledit premier moyen d'antenne hyperfréquence (31₆₁) comprend une sonde, et ledit second moyen d'antenne hyperfréquence (31₆₂) comprend deux sondes placées dans le même plan, dont des parties d'extension sont dans une relation orthogonale.
13. Dispositif de décalage de phase selon l'une des revendications 7 à 9, dans lequel ledit moyen de circuit de mélange (32, 33) comprend un circuit hybride de 3dB déphasé de 90° (32).
14. Dispositif de décalage de phase selon l'une des revendications 7 à 9, dans lequel ledit moyen de circuit de mélange (32) comprend le circuit terminal à deux branches.

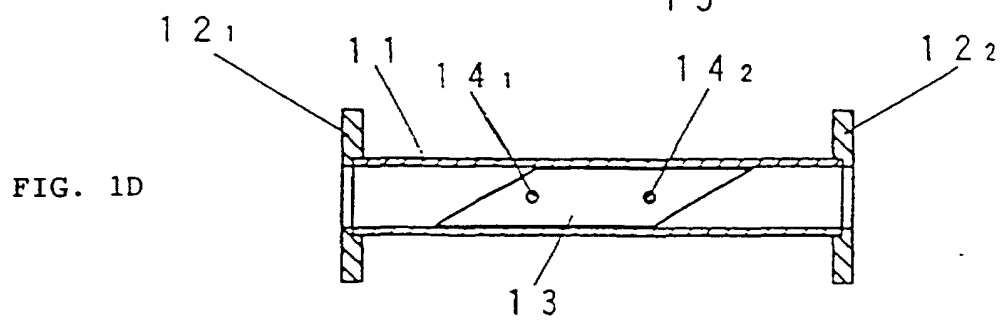
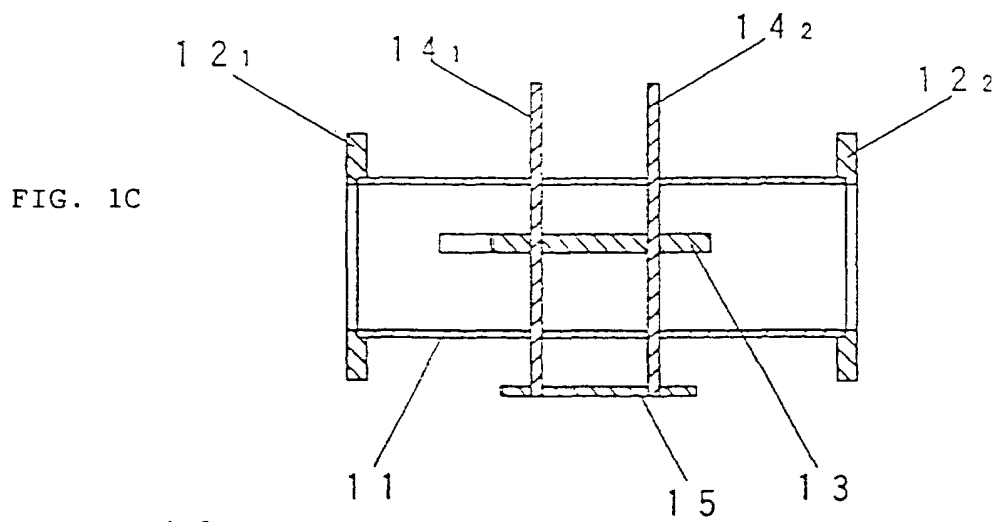
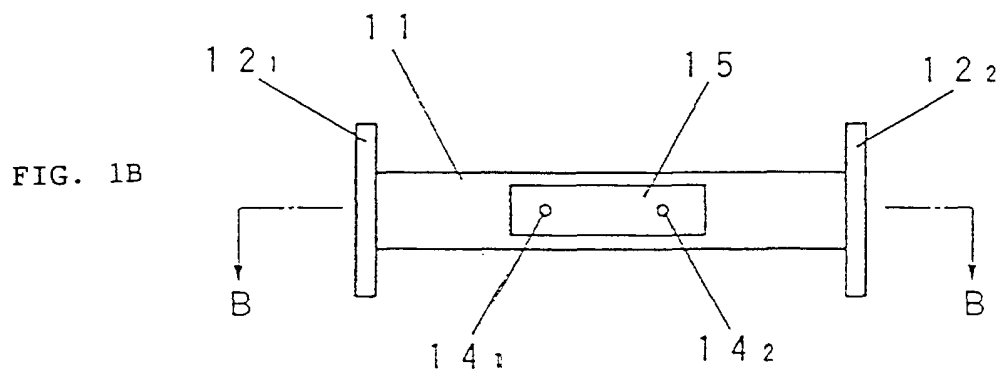
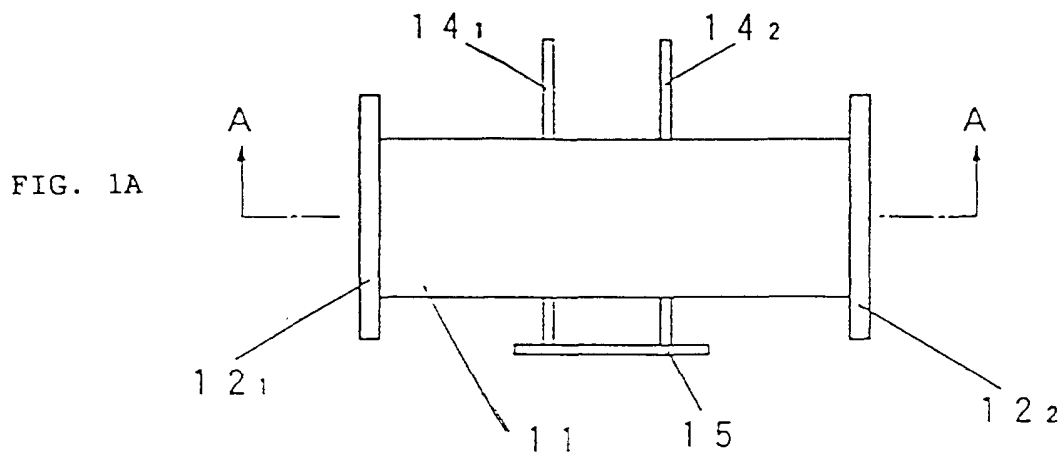


FIG. 2

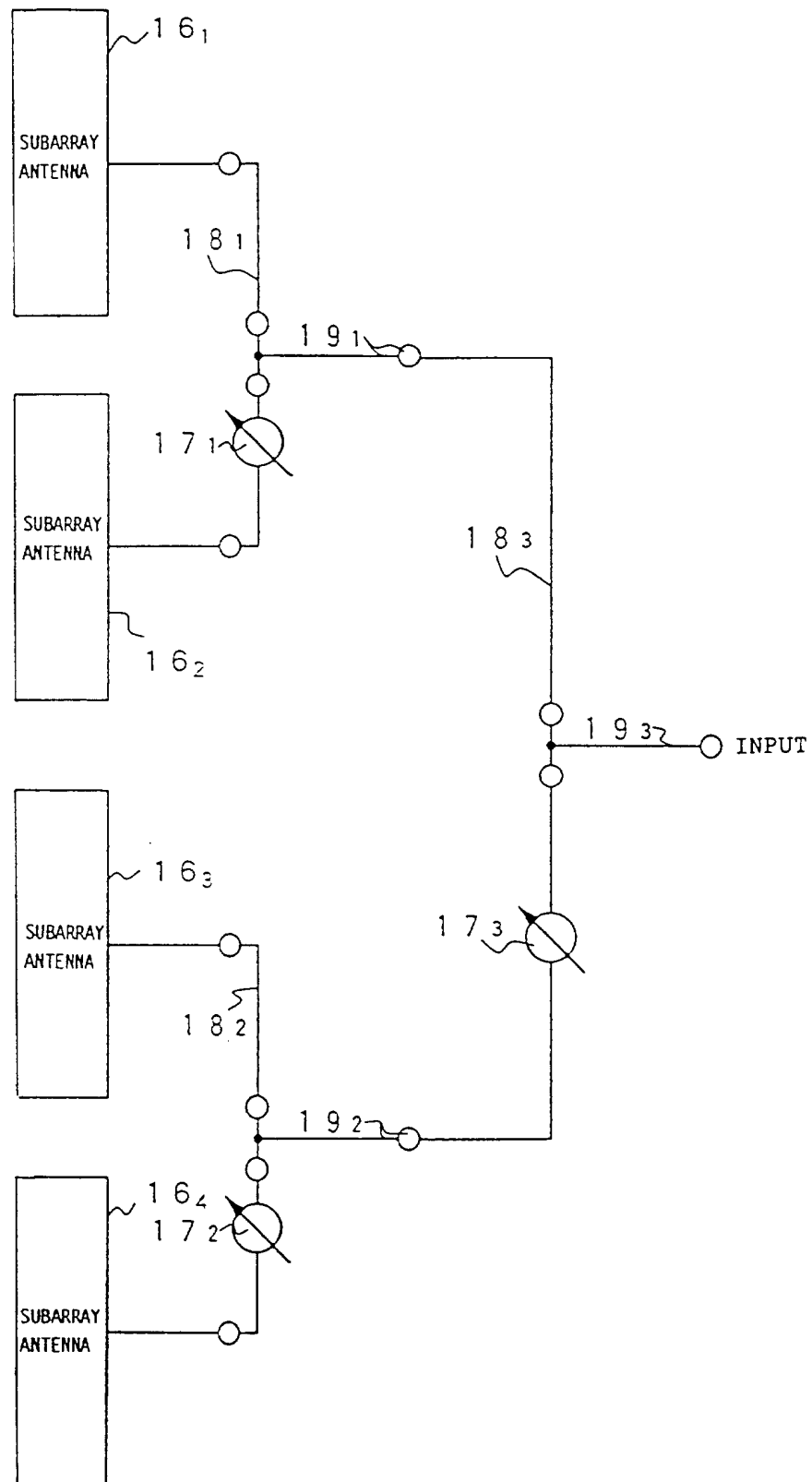


FIG. 3

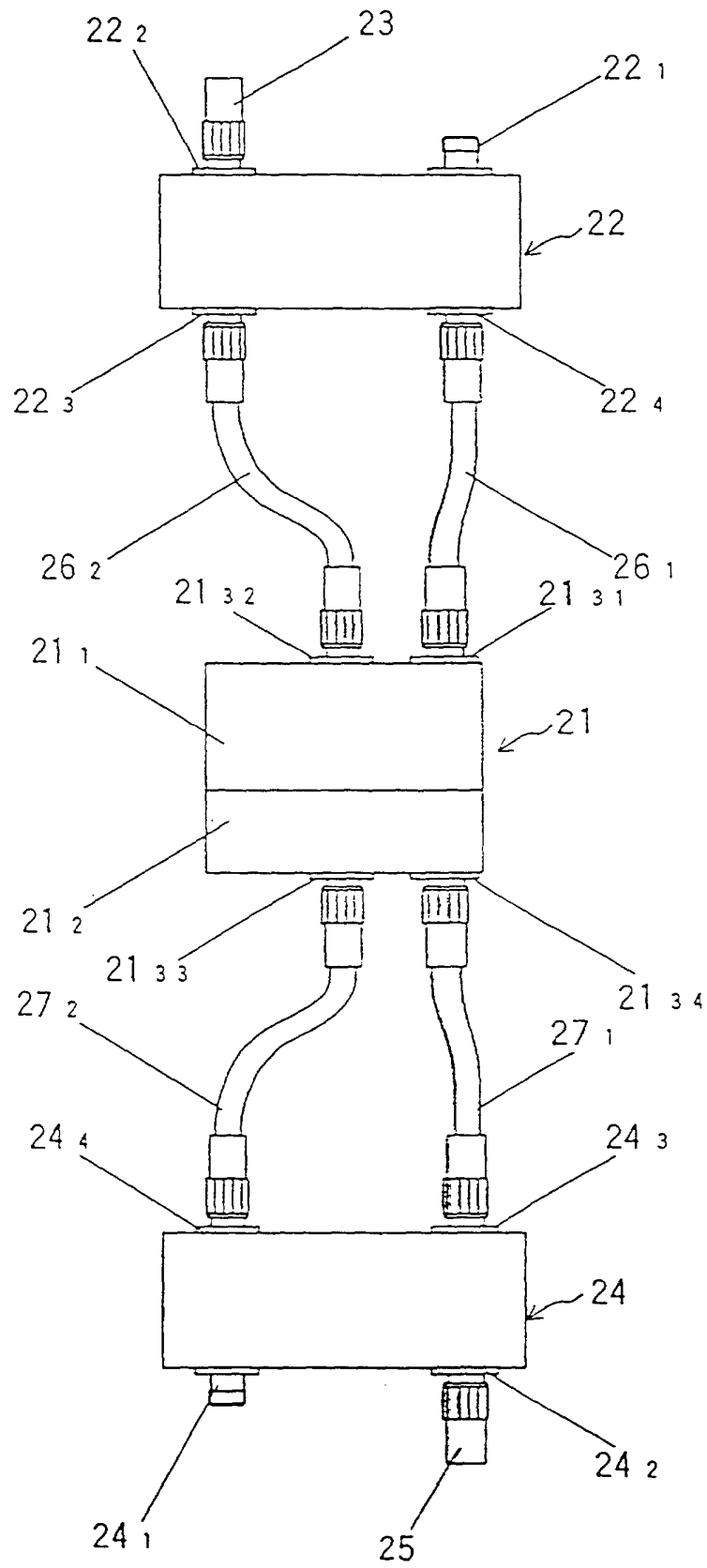


FIG. 4

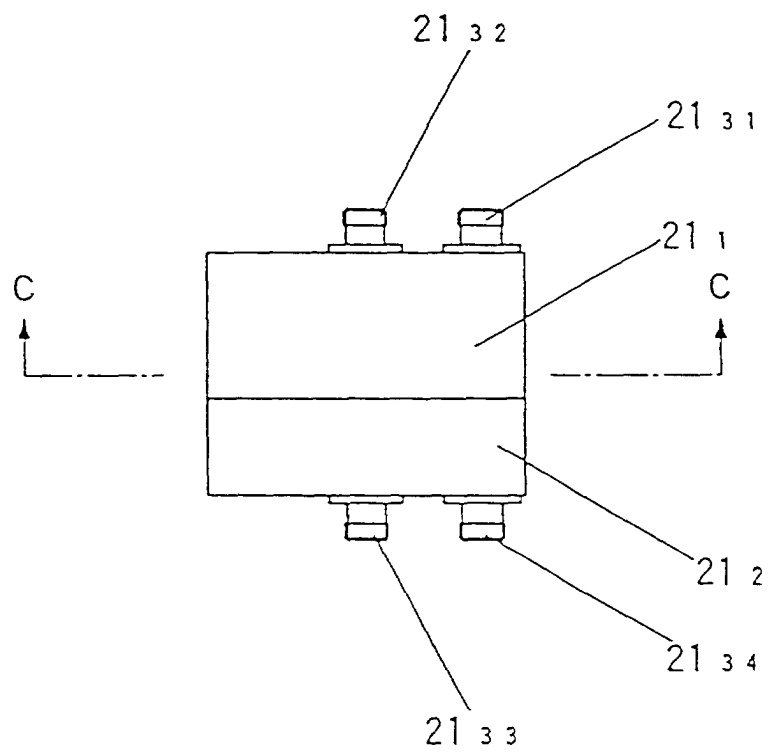


FIG. 5

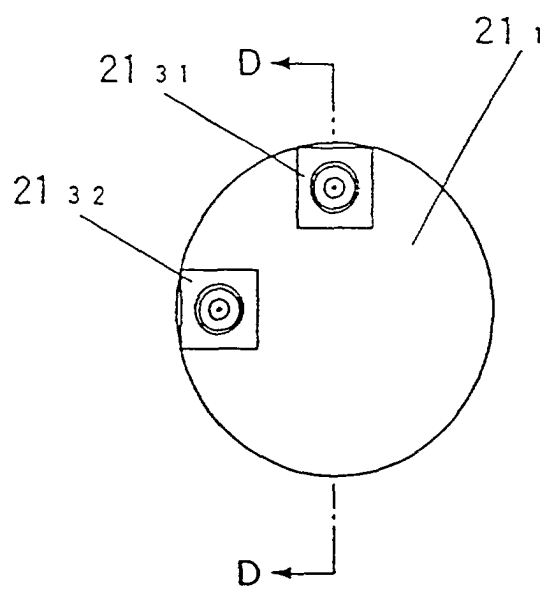


FIG. 6

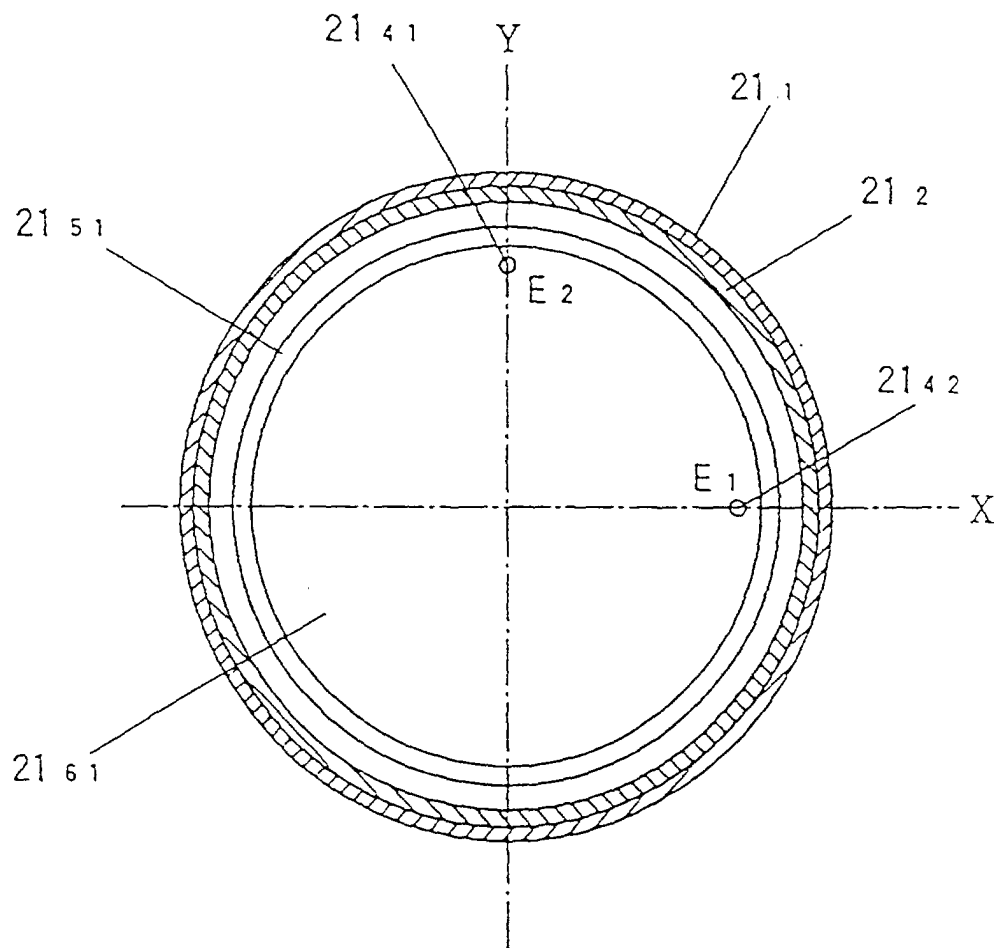


FIG. 7

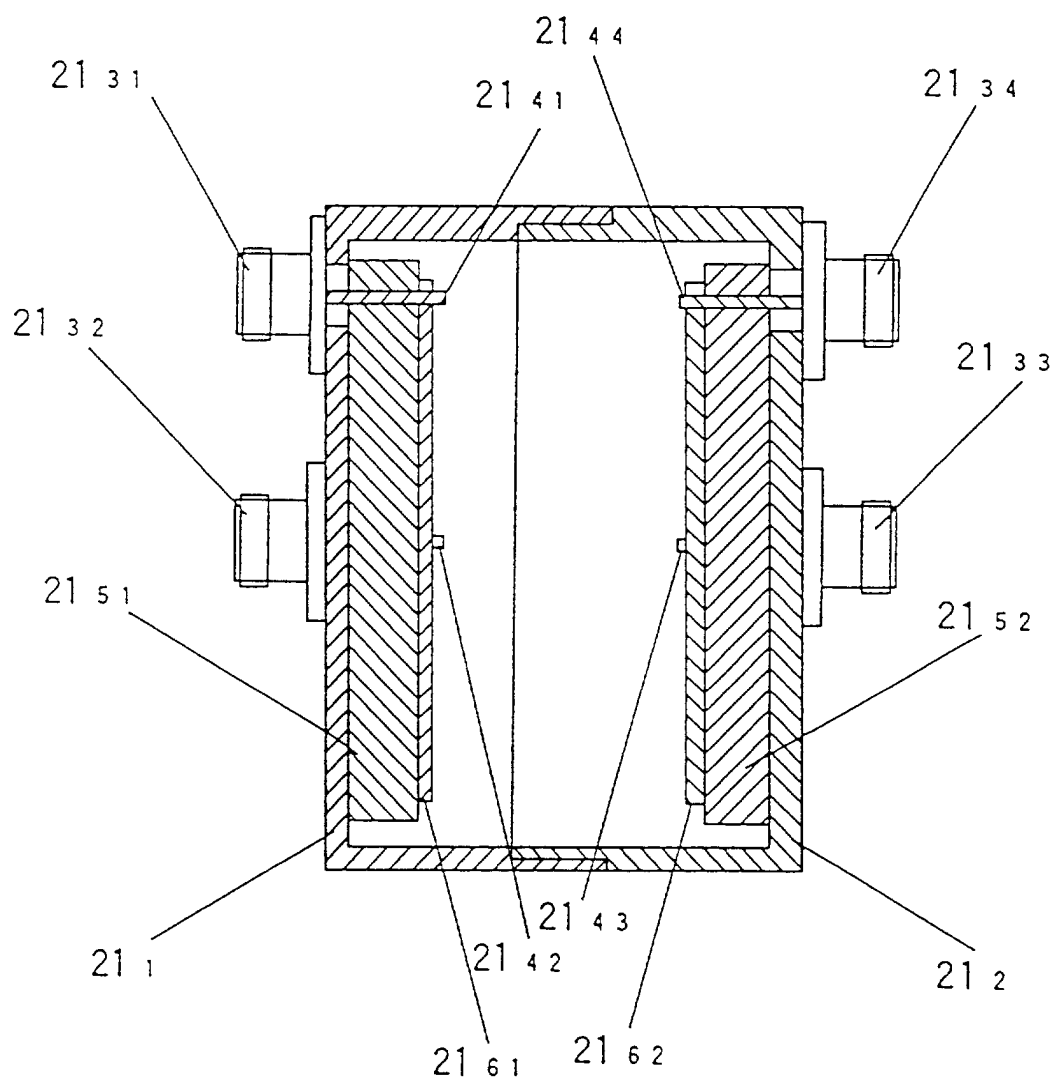


FIG. 8

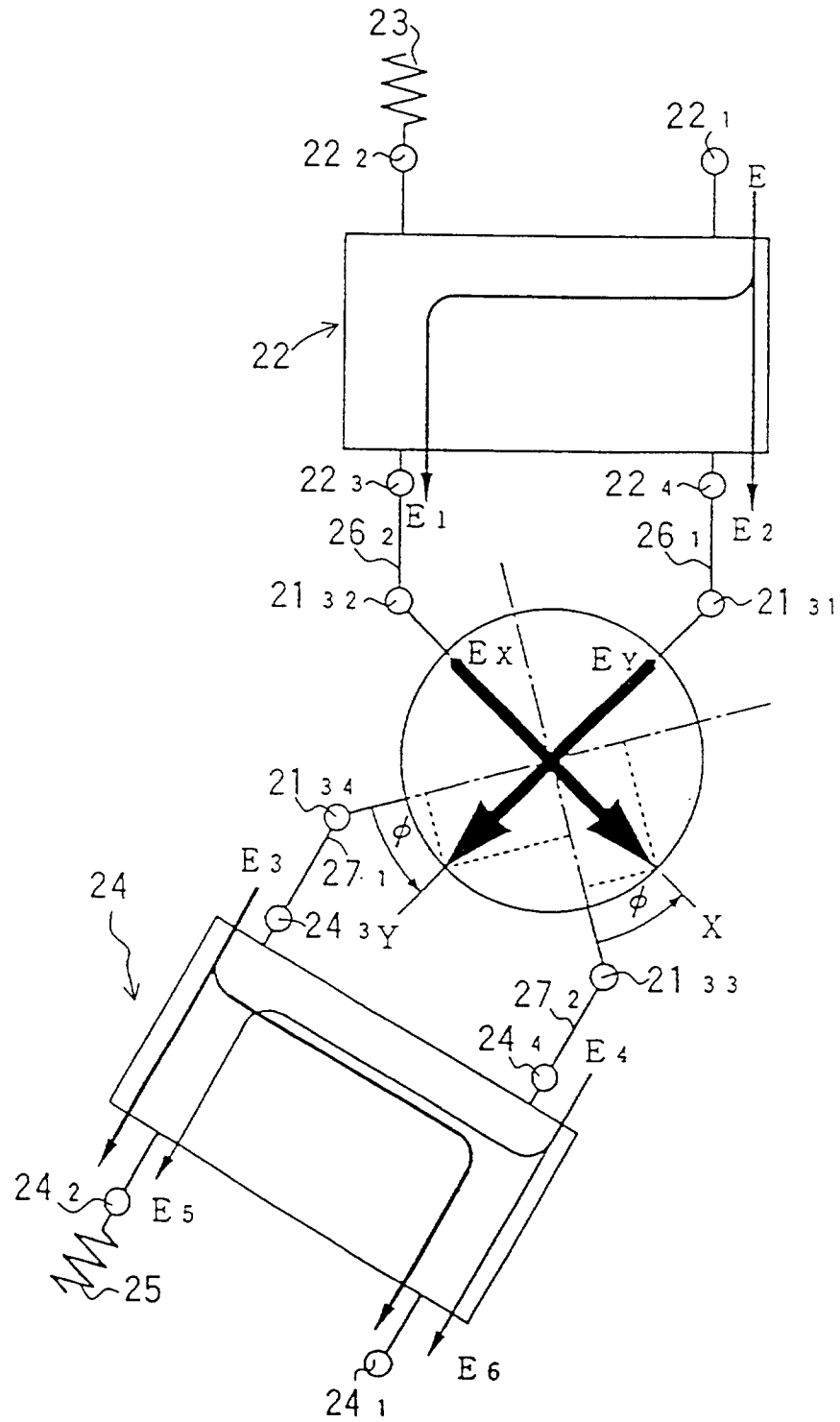


FIG. 9

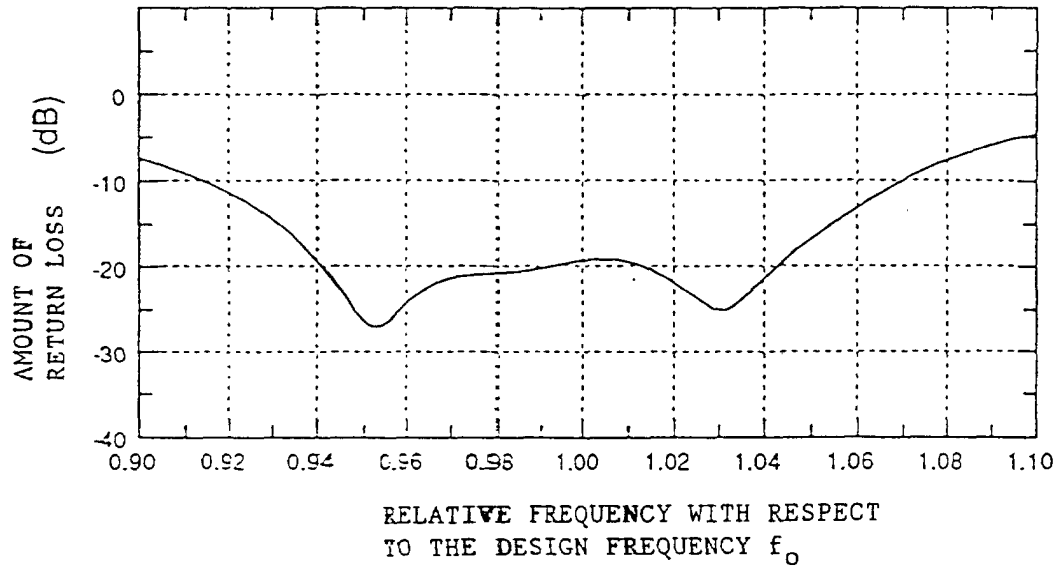


FIG. 10

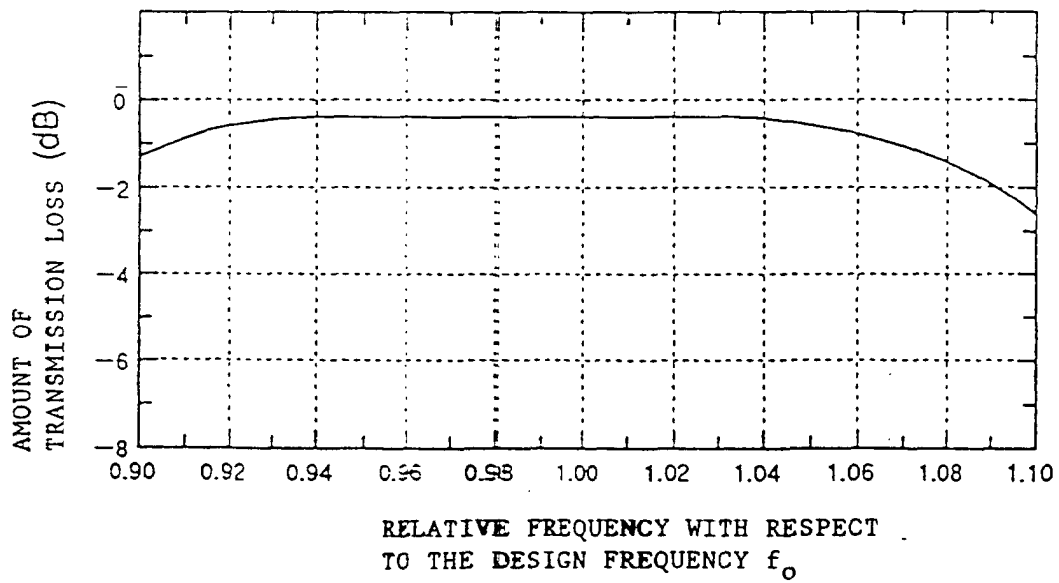


FIG. 11

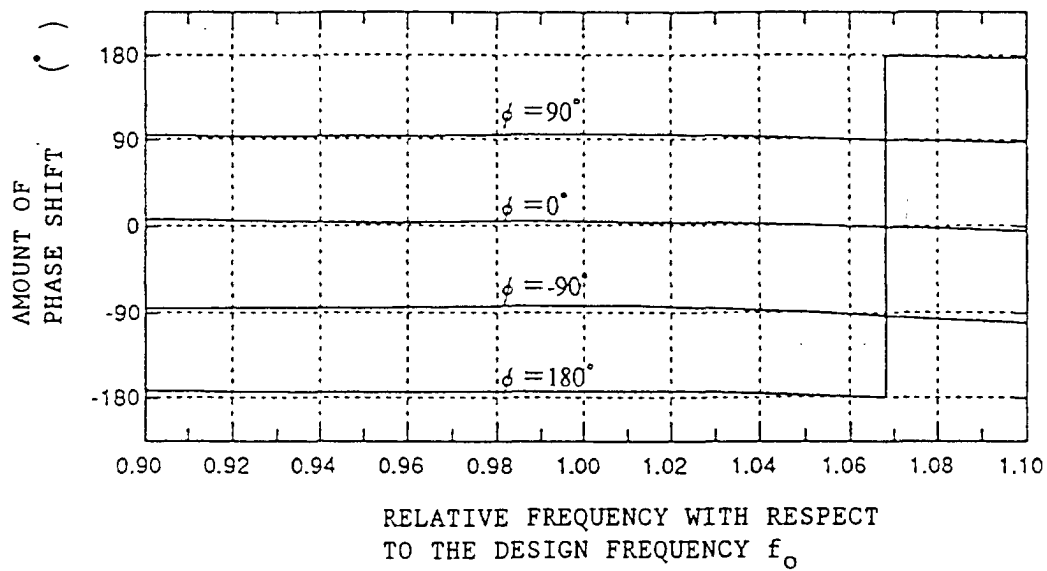


FIG. 12

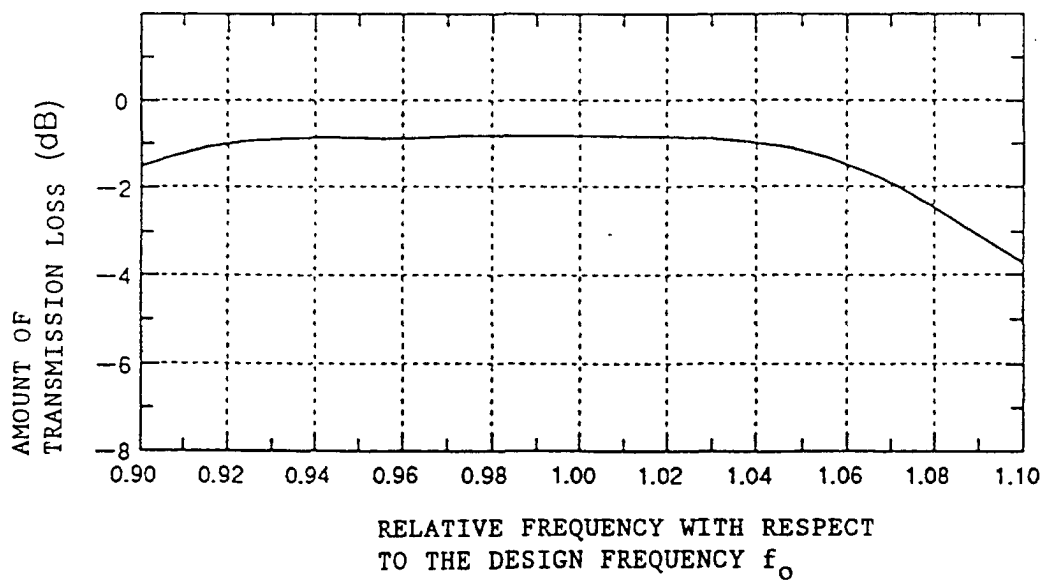


FIG. 13

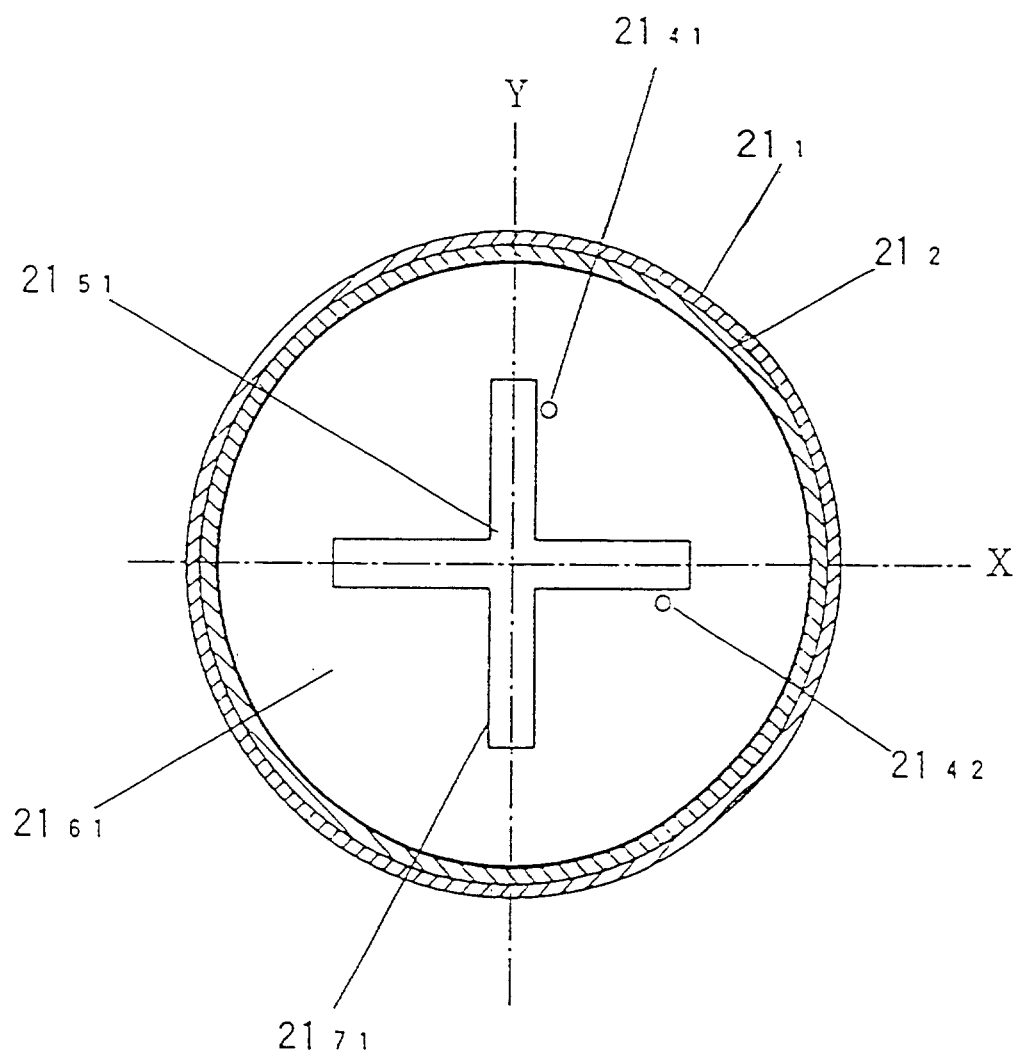


FIG. 14

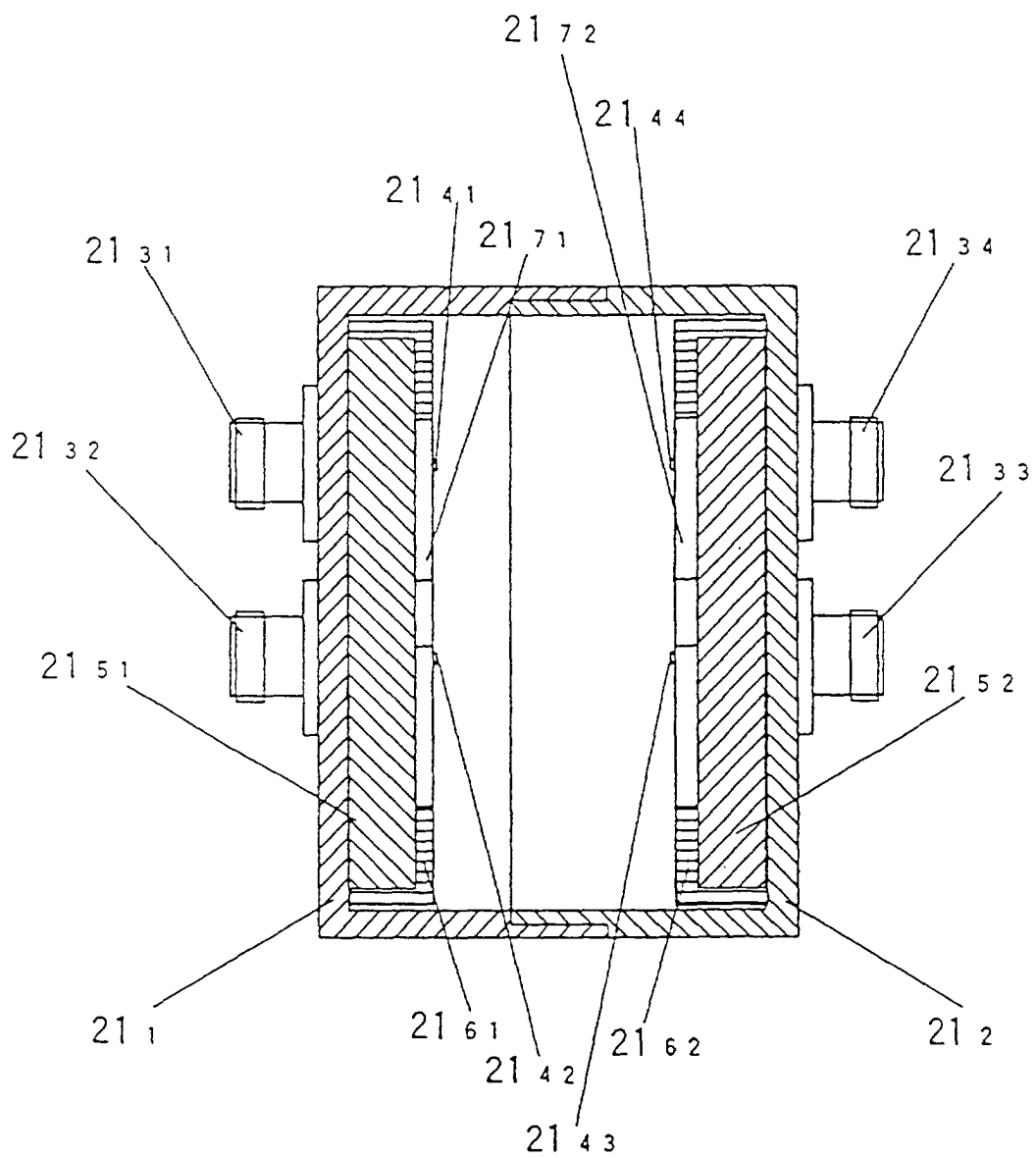


FIG. 15

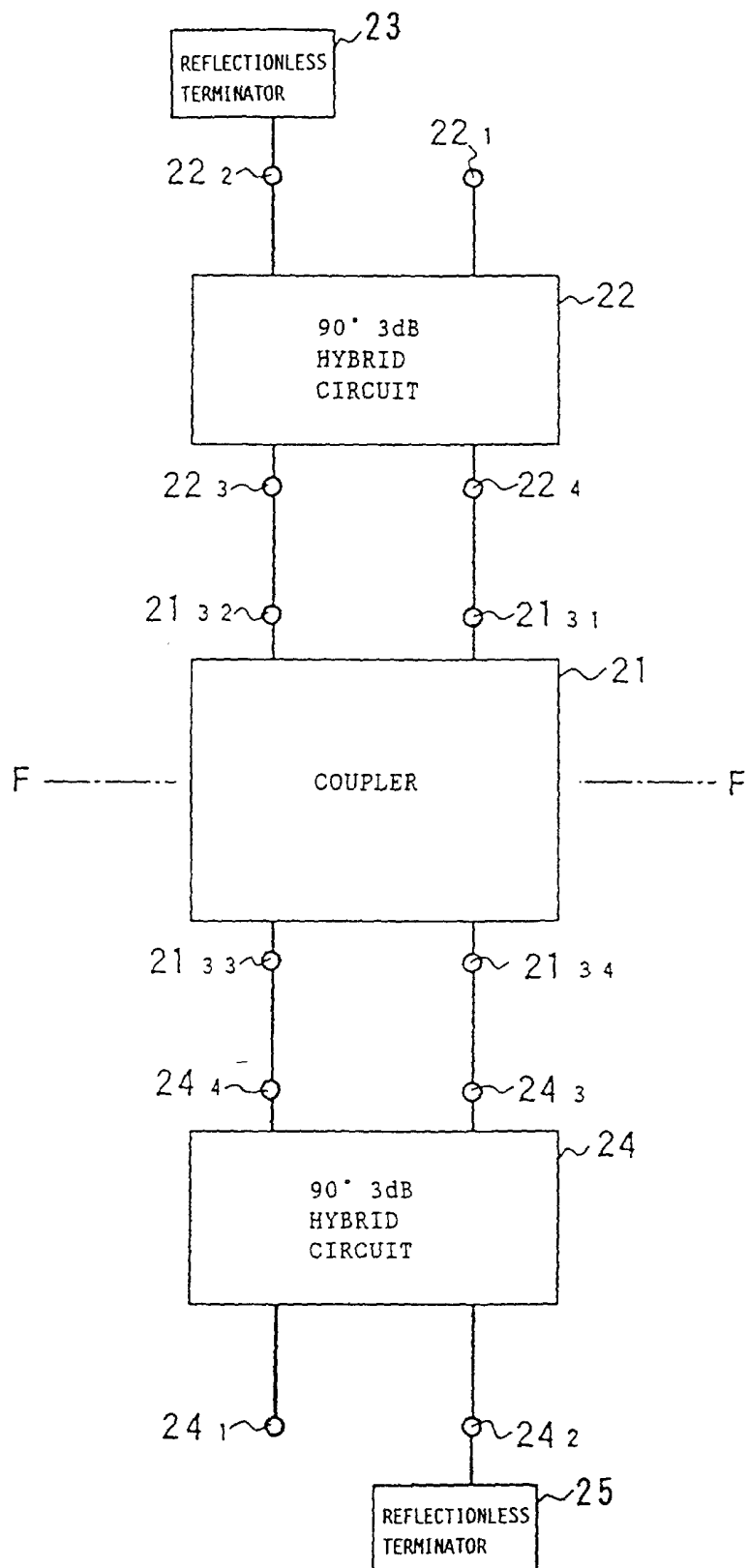


FIG. 16

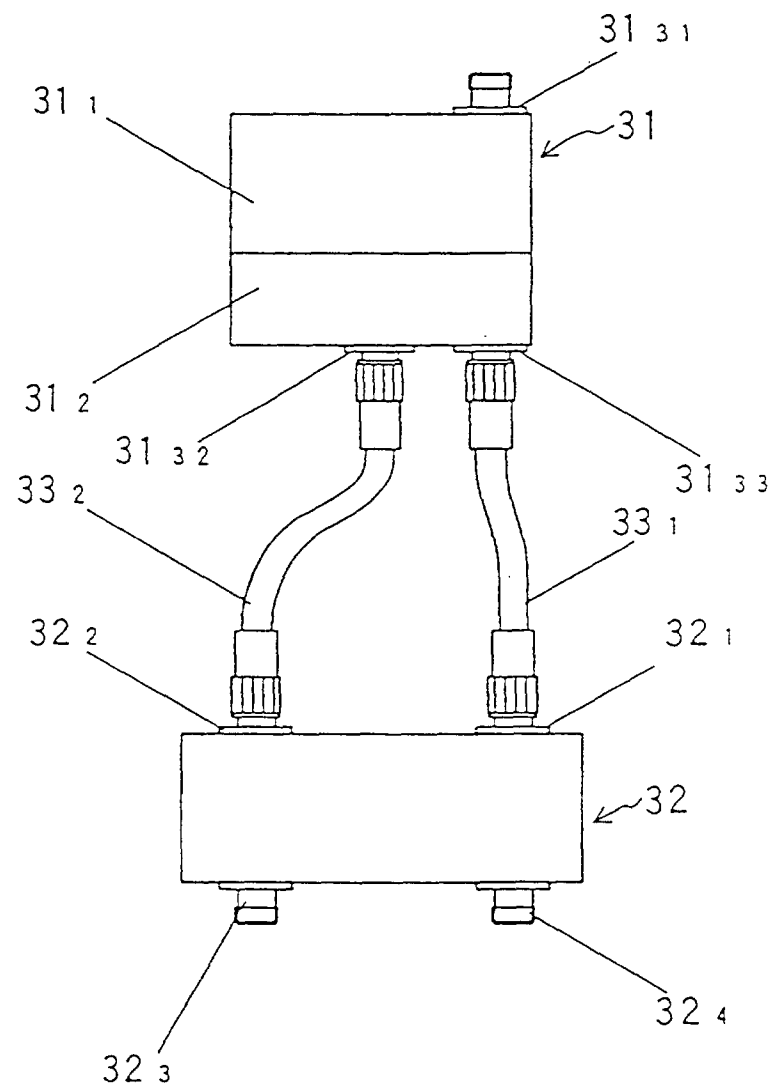


FIG. 17

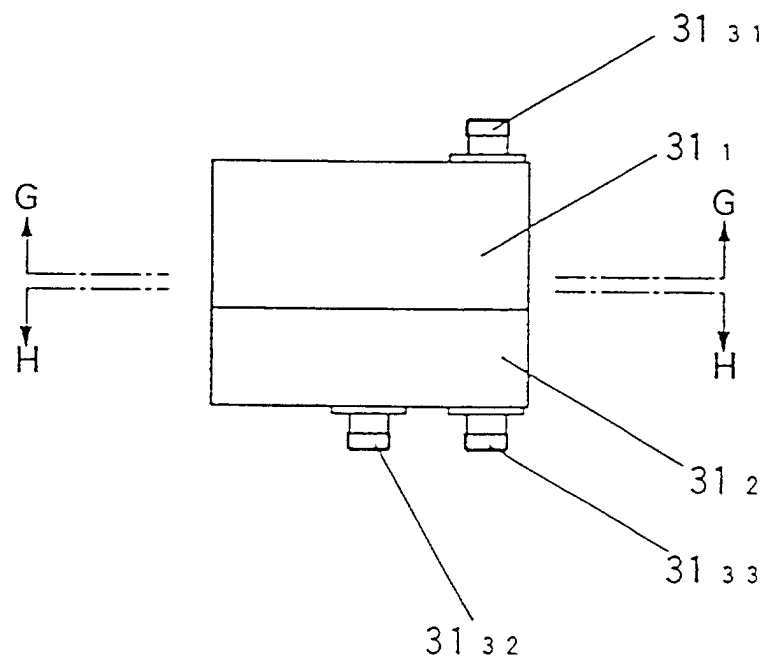


FIG. 18

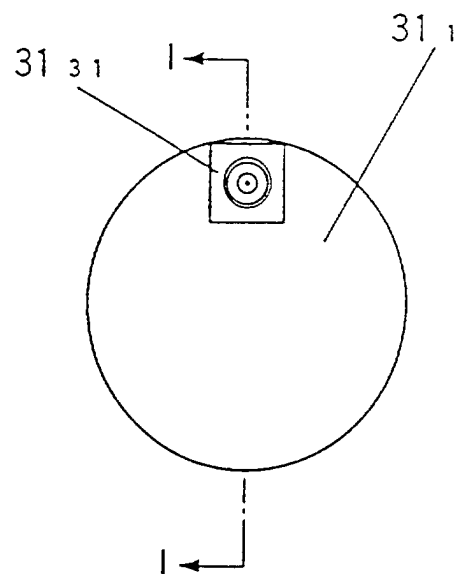


FIG. 19

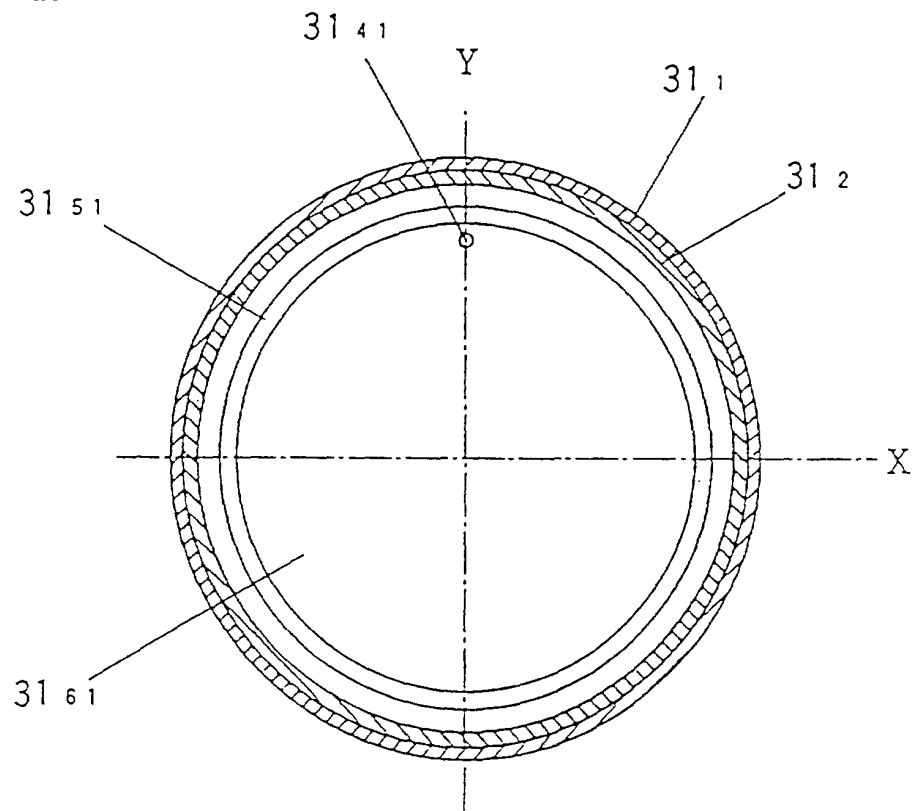


FIG. 20

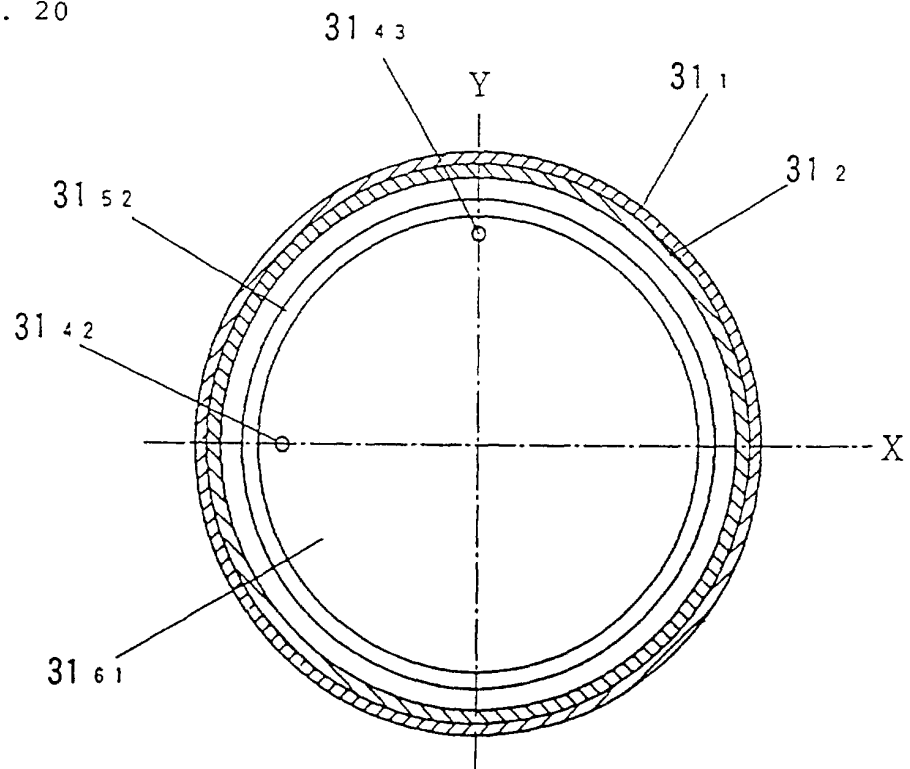


FIG. 21

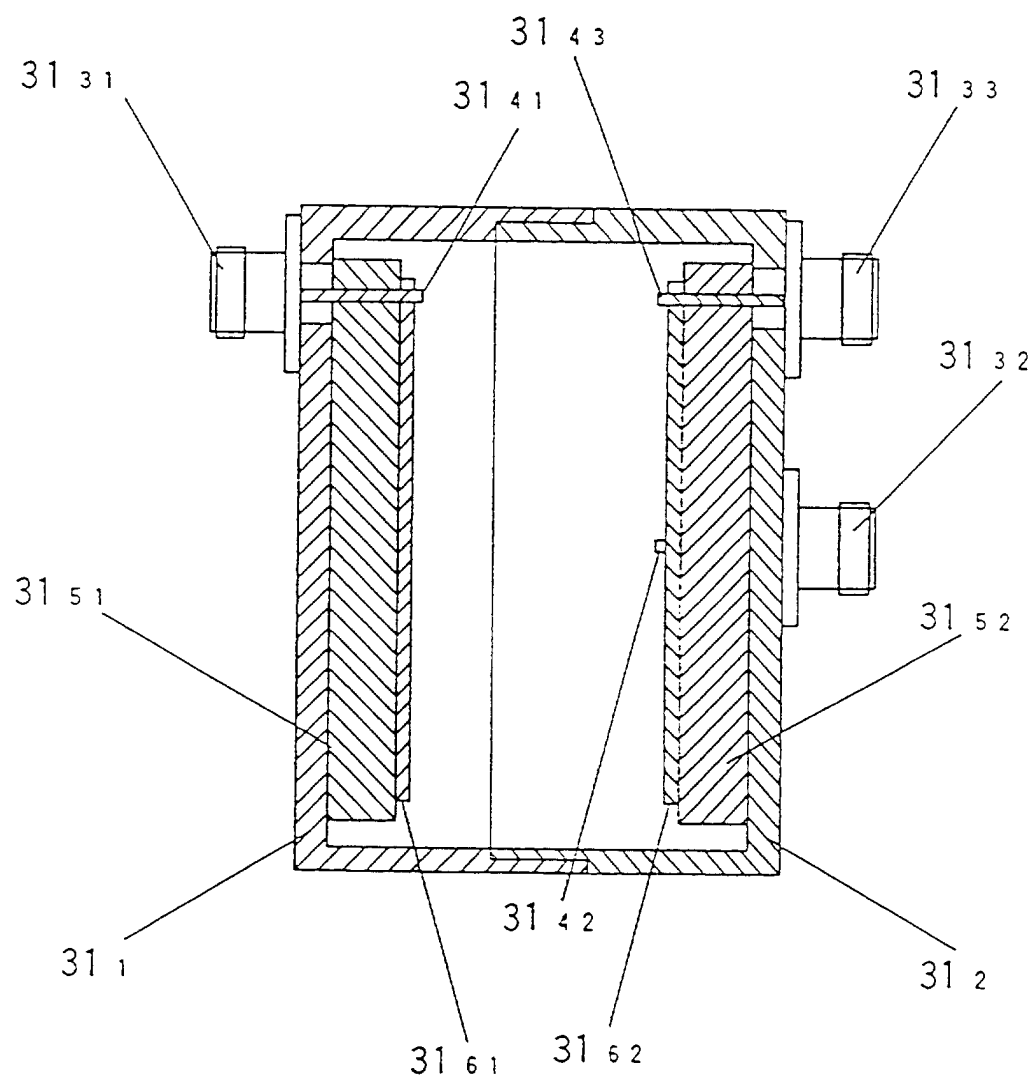


FIG. 22A

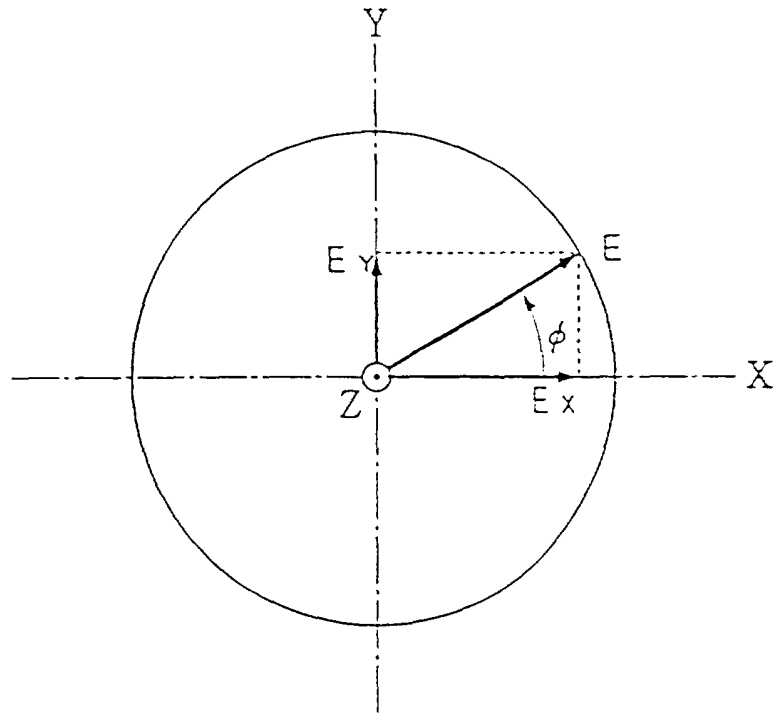


FIG. 22B

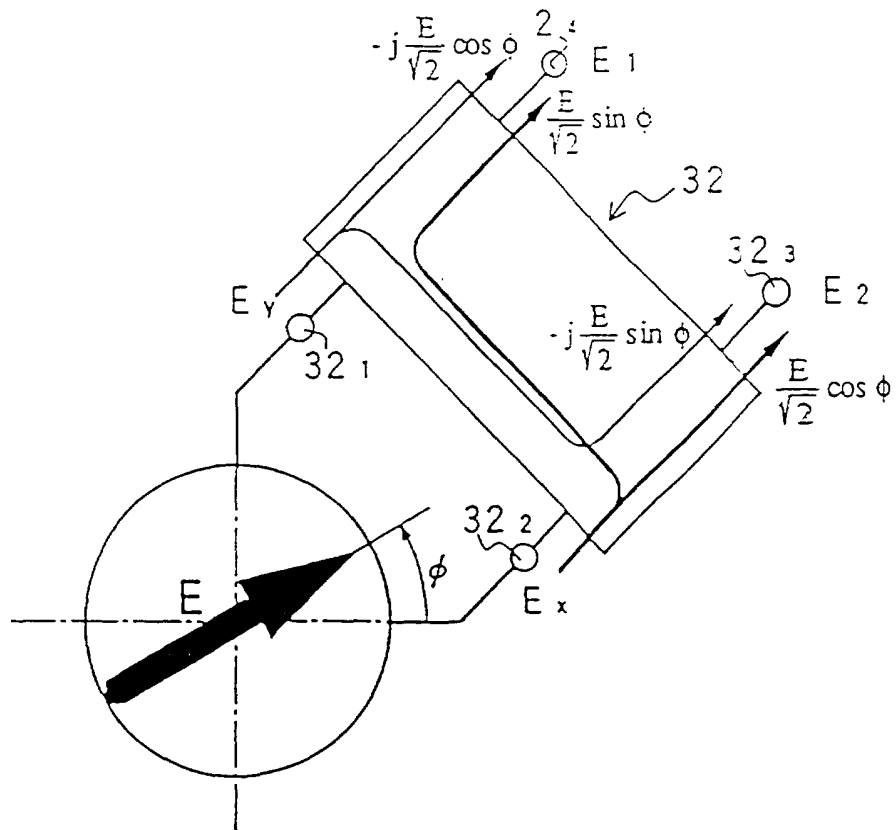


FIG. 23

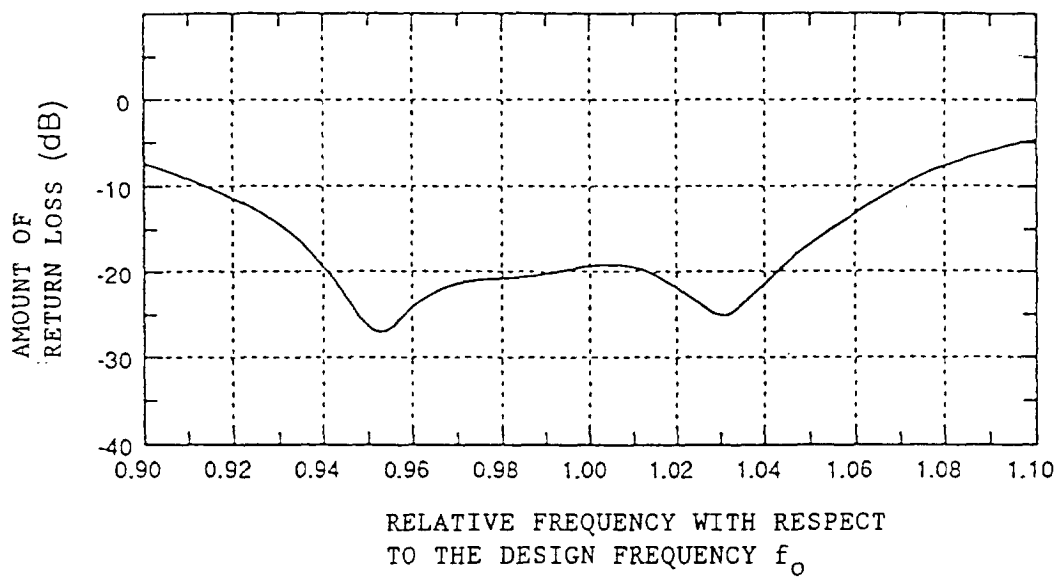


FIG. 24

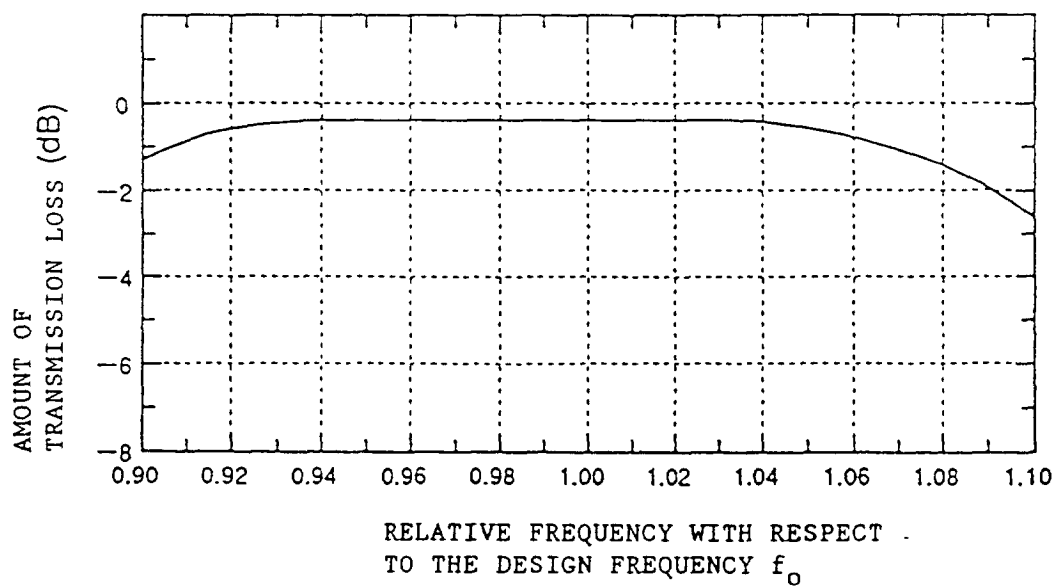


FIG. 25

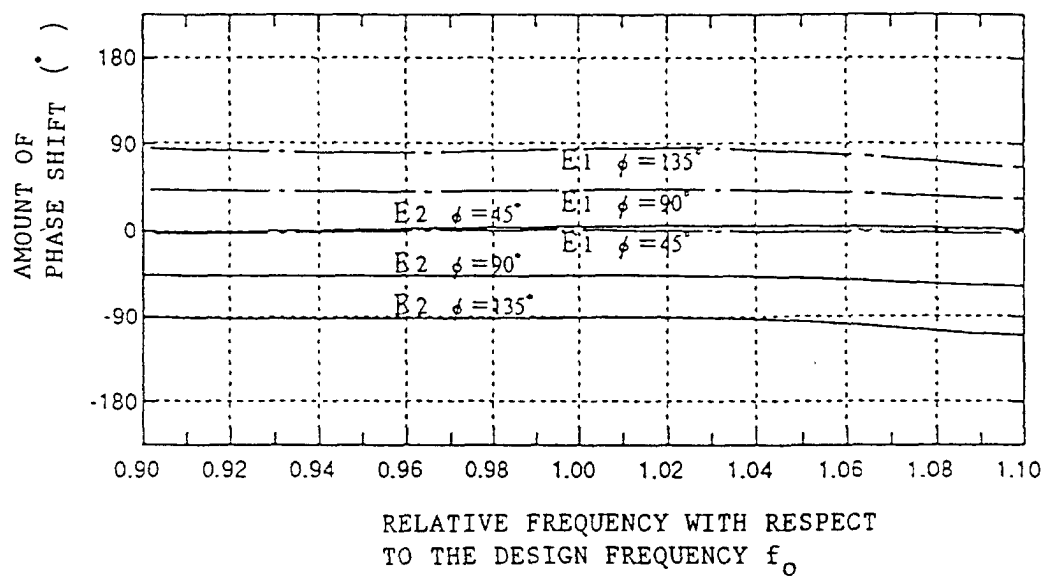


FIG. 26

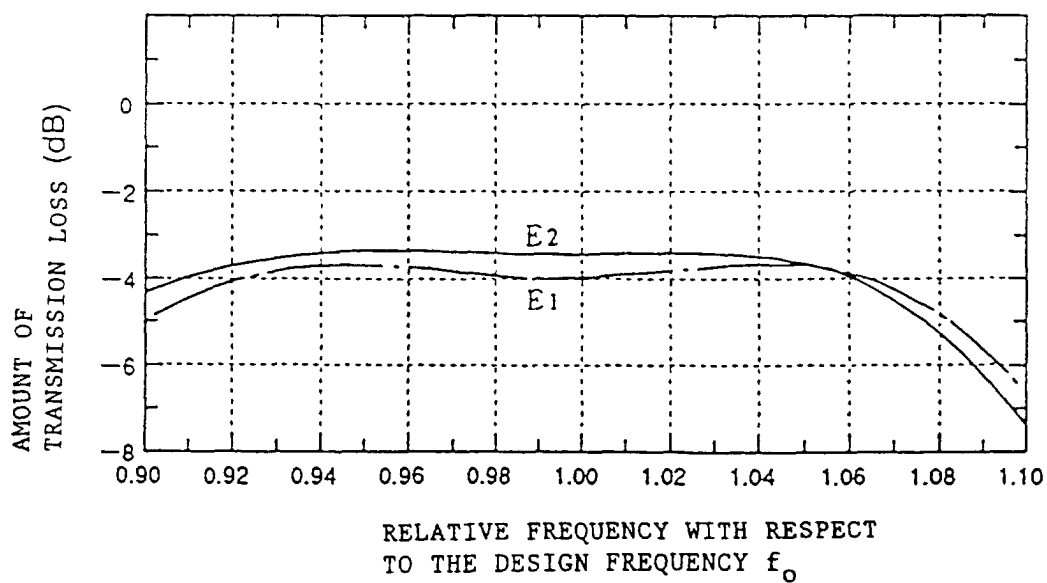


FIG. 27

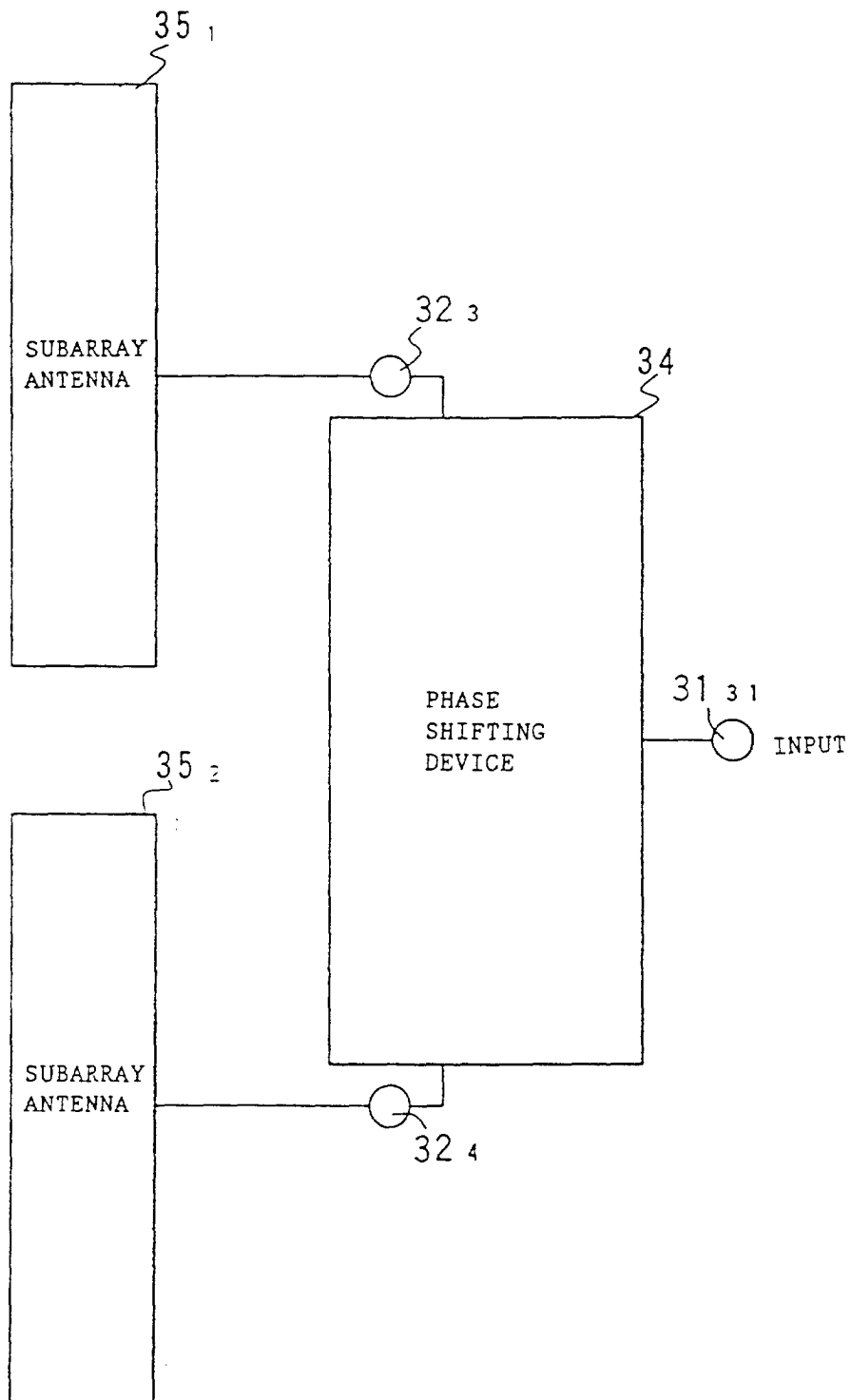


FIG. 28

