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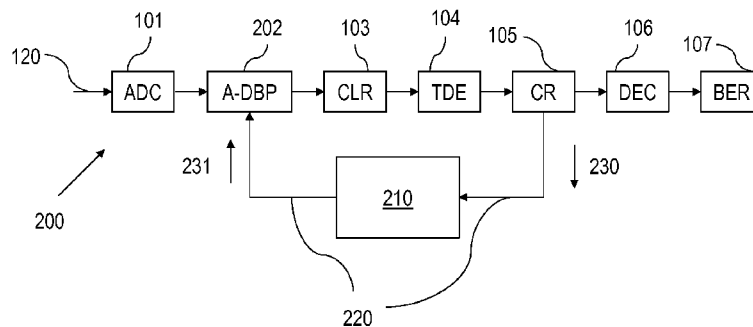
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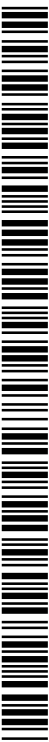
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(54) Title: METHOD, DEVICE AND COMMUNICATION SYSTEM FOR REDUCING OPTICAL TRANSMISSION IMPAIRMENTS

Fig.2a



(57) Abstract: A method and device is provided for reducing optical transmission impairments, particularly nonlinear effects, of at least one link. Said method comprising the following steps: extracting a phase information ($\Delta\theta$) from an optical signal (120) received via that at least one link, determining a nonlinear coefficient (γ), associated with the at least one link, based on the phase information ($\Delta\theta$), applying a control mechanism (202) using the nonlinear coefficient (γ). Furthermore, a communication system is suggested comprising said device.



DescriptionMethod, device and communication system for reducing optical transmission impairments

5

The invention relates to a method, to a device and to a communication system for reducing optical transmission impairments.

10 Transmission impairments in optical fiber can be divided into two categories: linear and nonlinear impairments. Linear impairments include chromatic dispersion (CD), polarization-mode dispersion (PMD), symbol timing offset and optical filtering. Nonlinear propagation impairments
15 (some of them are induced by the "Kerr effect") include self-phase modulation (SPM), cross-phase modulation (XPM), four-wave mixing (FWM) and nonlinear phase noise (NLPN). Especially with advanced modulation formats, the influence of fiber transmission impairments is of high interest and
20 nonlinear effects represent the most severe limitation in increasing the product bandwidth and distance in high speed long haul optical communication.

Various methods of compensating fiber transmission
25 impairments have been investigated in recent areas, both in optical and electronic domain. The implementations of all-optical methods are practically expensive, less flexible and complex to implement. On the other hand, with the development of coherent receivers based on Digital Signal
30 Processing (DSP), electronic compensation techniques have emerged as the promising techniques for long-haul optical data transmission. After coherent demodulation the signals can be sampled and processed by DSP to compensate for fiber transmission impairments. This digital compensation is
35 considered of importance for mitigation of fiber transmission impairments as it can offer great flexibility and adaptation.

By solving the nonlinear Schrödinger equation, the optical signal amplitude and phase can be estimated at each point of the fiber. Based on the inverse mathematical solution of the nonlinear Schrödinger equation a compensating algorithm has been proposed as a universal technique for jointly compensating linear and nonlinear impairments which is referred to as Digital Back Propagation (DBP). The nonlinear coefficient γ ("Gamma") and the effective length of the fiber are exemplary parameters of DBP to be adjusted and optimized.

In [Asif et al., "Optimized digital backward propagation for phase modulated signals in mixed-optical fiber transmission links", 25 October 2010/Vol. 18, No. 22/OPTICS EXPRESS 22796] a parametric optimization of a Digital Backward Propagation algorithm for mitigating fiber transmission impairments is proposed and numerically demonstrated for phase modulated signals in mixed-optical fiber transmission links.

In next generation optical transmission systems (characterized in particular by the functional combination of fiber optics technology together with Internet protocols), phase modulated optical signals will be used at a high symbol rate. This means nonlinear transmission impairments like Self-Phase Modulation (SPM) are limiting effects and therefore DBP may lead to a significant improvement of transmission performance.

The DBP method assumes full knowledge of the link (i.e. knowledge of the fiber span configurations and parameters) in terms of fiber types, measured optical powers, fiber lengths, etc. Unfortunately, such information is usually only partially available. Therefore, based on an accurate inversion of the optical propagation equation, DBP cannot

provide reliable distortion compensation if a precise description of the link is missing.

Optical systems may consist of tens or even hundreds of
5 links. Hence, it is quite unlikely that an accurate system
description can be obtained. Moreover, even assuming a
perfect knowledge of the link, the values of the optical
power along the system cannot be measured correctly. This
causes a further degree of uncertainty whenever a DSP is
10 designed to compensate nonlinearities by applying DBP.

[T. Tanimura et al., "Semi-blind Nonlinear Equalization in
Coherent Multi-Span Transmission System with Inhomogeneous
Span Parameters", OSA/OFC/NFOEC 2010] discloses a digital
15 coherent receiver employing semi-blind dual-polarization
nonlinear compensator (DP-NLC), whereas a semi-blind
algorithm is proposed that optimizes the parameter values
of a nonlinear compensator based on limited prior
information of the link. Concerning this, effective Q-
20 factors (which are related to the signal quality) are
derived by analyzing the bit errors rate (BER) after
polarization de-multiplexing, frequency offset
compensation, a Viterbi & Viterbi carrier recovery, symbol
decision and differential decoding. Quality parameters are
25 adjusted based on the signal, wherein such quality
parameters are fed to the nonlinear compensator. An
optimization of the parameter values, however, is only
possible after BER determination, which causes time delays.

30 The **problem** to be solved is to provide an improved optical
performance monitoring technique, particularly an improved
and robust solution for DBP implementation.

This problem is solved according to the features of the
35 independent claims. Further embodiments result from the
depending claims.

In order to overcome this problem, a method is provided for reducing optical transmission impairments, particularly nonlinear effects, of at least one link, comprising the following steps:

5

- a) extracting a phase information from an optical signal received via the at least one link,
- b) determining a nonlinear coefficient, associated with the at least one link, based on the phase information,
- 10 c) applying a control mechanism based on the nonlinear coefficient.

This solution represents an optical performance monitoring technique to estimate the nonlinear coefficient γ (Gamma) of a homogeneous link.

15

A "fiber optic link" may be a transmitter, receiver, cable assembly or an interface that can transmit information between two points.

20

A link may also be a fiber optic span in the sense of an optical fiber/cable terminated at both ends optionally including devices that add, subtract or attenuate optical signals.

25

Without any need for using a FEC (Forward Error Correction) module (i.e. BER analysis) in order to adjust the nonlinear coefficient γ this solution beneficially uses information which is already available after carrier recovery of the received signal which results in an accelerated determination of a correct or an improved nonlinear coefficient γ .

30

In an embodiment, the steps a) to c) will be repeated until the nonlinear coefficient value reaches or exceeds a value or threshold. The value can be a predetermined value.

35

In a further embodiment, the steps a) to c) will be repeated until the nonlinear coefficient value reaches an optimal value. Beneficially, after steps a) to c) have stopped, the bit error rate (BER) of an information
5 transmission over the link or span may have reached its minimum.

In another embodiment, the control mechanism comprises a Digital Backward Propagation algorithm (DBP). DBP is a
10 universal technique for jointly compensating linear and nonlinear impairments.

In a further embodiment, the phase information is extracted after a carrier recovery of the received optical signal. By
15 processing the signal after carrier recovery the determination of an improved nonlinear coefficient γ can be accelerated.

In a next embodiment, a cost function is derived based on
20 the extracted phase information and an optimization algorithm is applied in connection with that cost function to determine the nonlinear coefficient γ . By applying the optimization algorithm for the cost function, it allows speeding up a convergence to correct or tune the nonlinear
25 coefficient γ towards its optimal value. The optimization may indicate, that only an absolute or local minimum is remaining.

It is also an embodiment that the extracted phase
30 information comprises a spreading of receiving symbols being part of that received coherent optical signal, and that the determination of the nonlinear coefficient γ is such that a reduced spreading of the receiving symbols is achieved. Spreading can be understood as a statistical
35 function, also known as "scattering" or "inter-symbol interference".

Pursuant to another embodiment, the respective spreading of the received symbols comprises respective phase differences between the received symbols and respective transmitted symbols which are derived either with or without a training sequence. A "blind method" (using symbols which have
5 already been decided or classified) or a data aided method (using training symbols) are both valid.

According to an embodiment, the received optical signal is
10 a coherent signal based on a 16 QAM modulation, wherein

- the 4th power is applied to the received optical signal,
- the respective phase differences are derived from a 4th power signal,
- 15 - the cost function, based on those derived phase differences, is defined as

$$CF = [\delta\theta_1 + \delta\theta_3] * (1/R_2) + \delta\theta_2 * (1/R_1 + 1/R_3)$$

20 wherein

- $\delta\theta_1$, $\delta\theta_2$, and $\delta\theta_3$ represent a standard deviation for each of the respective phase differences θ_1 to θ_3 , and
- R_1 , R_2 and R_3 represent the radii of the 16 QAM
25 constellation.

According to another embodiment, the optimization algorithm is based on the steepest descent algorithm.

30 In a next embodiment the steepest descend algorithm is defined as

$$\gamma(i + 1) = \gamma(i) + \mu\Delta\gamma(i)$$

35 wherein

- i is an index of a discrete time;

- $\gamma(i+1)$ represents the value of the nonlinear coefficient at an iteration (i+1);
 - $\gamma(i)$ represents the value of the nonlinear coefficient at a preceding iteration step (i);
 - 5 - μ represents the convergence factor, comprising an effective fiber length L_{eff} and a channel power P;
 - $\Delta\gamma(i) = \partial CF(\gamma)/\partial\gamma$ is a gradient of the cost function over a nonlinear coefficient.
- 10 The effective fiber length may be derived according to the following exemplary relation:

$$L_{eff} = \frac{1 - \exp(-\alpha L)}{\alpha},$$

15 wherein

α is a fiber attenuation defined in [Np/km].

According to a next embodiment, the optimization algorithm
20 starts by calculating two values of the cost function corresponding to two different values of the nonlinear coefficient γ , and wherein the first starting value of the nonlinear coefficient is represented by a selected initial value.

25

As the proposed method represents a robust optimization algorithm any kind of value can be selected as initial starting value, preferred based on experience and possible real physical values.

30

Pursuant to yet an embodiment, the nonlinear coefficient γ is refined as an n-dimensional nonlinear coefficient, representing n single links, wherein the n-dimensional nonlinear coefficient is determined by an n-dimensional
35 calculation. According to this embodiment, optical transmission impairments of more than one optical link can be compensated. Beneficially, the proposed solution can be

applied in future network scenarios where optical signals are transmitted via several links.

The problem stated above is also solved by a device
5 comprising a control mechanism for reducing optical transmission impairments, particularly nonlinear effects, of at least one link which can be connected to the device and a processor unit. The processor unit is arranged such that the following steps can be executed or processed:

- 10 a) extracting a phase information from an optical signal received via that at least one link,
b) determining a nonlinear coefficient, associated with the at least one link, based on the phase information,
c) applying the control mechanism using the nonlinear
15 coefficient.

According to an embodiment, the device is a communication device, in particular a or being associated with a receiver for optical signals.

20

The problem stated supra is further solved by a communication system comprising the device as described herein.

25 Embodiments of the invention are shown and illustrated in the following figures:

Fig.1 shows a block diagram of an optical coherent receiver based on digital signal processing (DSP);

30

Fig.2a shows a block diagram of a DSP-based coherent receiver according to the proposed solution;

Fig.2b shows an exemplary flow chart of the proposed
35 solution;

- Fig.3 shows a histogram of the derived phase difference of a 16 QAM modulated signal;
- Fig.4 shows a histogram of the derived phase difference of the 4th power of a 16 QAM modulated signal;
- Fig.5 shows a 16 QAM constellation diagram to the 4th-power;
- Fig.6 exemplarily shows a derived cost function CF for determining an optimized value of the nonlinear coefficient γ based on a 16 QAM modulated signal over a standard single-mode fiber;
- Fig.7 shows an example of a derived cost function based on a 16 QAM modulated signal over a large-effective area pure silica core fiber;
- Fig.8 and 9 each shows an example concerning the quality performance of the proposed method;
- Fig 10 to 13 each shows a further example of a signal constellation diagram applied to the 4th power, based on a further exemplary modulation format.

With reference to **Fig.1**, a common used DSP-based coherent receiver is exemplarily depicted according to prior art. In a first step a received signal 120 is digitally converted by a block of four analog-to-digital converters 101. In a following step bulk chromatic dispersion and nonlinear effects are compensated by a Digital Back-Propagation (DBP) algorithm implemented by a DBP Module 102. After a time synchronization provided by a clock recovery module 103, a signal polarization de-multiplexing is performed by a time domain equalizer 104, which can also be implemented in a carrier recovery module 105. The succeeding steps process

received coherent signals via the modules carrier recovery 105, decision making on received symbols 106 and estimation of a bit error rate 107.

5 The coherent receiver can be refined as a data-aided receiver (i.e. using training sequences (TS)). Nevertheless, the proposed method can also be realized by utilizing a receiver, which operates without training sequences (also referred to as "blind receiver").

10

The DBP algorithm or DBP module 102 requires a description of the link, which is used for back-propagation purposes. It is one of the advantages of the proposed solution that DBP can be used even by applying an arbitrary or incorrect
15 link description. An incorrect link description can result (among others) the following, statistically independent, sources of errors:

- the fiber length (which is possibly incorrect),
- 20 - the fiber type (which is possibly wrong) or
- the power levels (which can not be measured accurately)

Generally, it can be distinguished between homogeneous and
25 inhomogeneous links. Homogeneous links comprise equal fibers for all spans (an optical fiber/cable terminated at both ends which may include devices that add, subtract, or attenuate optical signals) which is the usual scenario for point-to-point connections. Inhomogeneous links are usually
30 found in meshed optical networks, where links comprising the same type of fiber can hardly be found.

In a homogeneous scenario, the error on estimating the length of a single link or span does not really cause a
35 problem as, after compensation of linear and nonlinear effects, this error will be averaged out - provided that the error is confined to a reasonable range. Errors of up

to 20% on the length specification do not induce any significant impairment, in case DBP is used.

On the other hand, in a meshed network or even on a single
5 link, an error concerning the type of fiber may not be averaged out, resulting in a system outage after DBP is applied.

Finally, in case of wrong measured power levels along the
10 link, the same disadvantage is valid as for estimating the wrong length of the fiber: if the error is uniformly distributed, DBP provides an improvement, otherwise the system performance deteriorates.

15 The solution presented herein solves the problem mentioned above: Exemplary results for a single homogenous link with a wrong estimation concerning the type of fiber but with exact knowledge of the CD value will be presented.

20 Examples for different types of fibers are:

- Large-Effective Area Pure Silica Core Fiber (LA-PSCF)
- Standard Single-Mode optical Fiber (SSMF)

25 The coherent receiver 200 shown in **Fig.2a** is based on the receiver according to Fig.1. In addition to Fig.1, a feedback connection 220 is provided between the carrier recovery module 105 and the DBP module which is now an adaptive DBP (A-DBP) module 202. Further, an adaptive
30 estimation module 210 is part of the feedback connection 220. A signal 230 which is the resulting outcome of the carrier recovery 105 is passed on to the Estimation Module 210, where the nonlinear coefficient parameter γ ("Gamma") is estimated or calculated respectively by processing the
35 internal signal 230 forwarded from the carrier recovery module 105 as will be described further below.

According to an embodiment of the proposed solution a wrong description with regard to the type of fiber can initially be provided to the adaptive DBP module 202. Additionally, a correct description of a dispersion parameter is provided to the adaptive DBP module 202. Apart from this, further knowledge being available concerning the link will be the number of spans and the individual length of the spans.

The adaptive algorithm according to the proposed solution, implemented in the adaptive estimation module 210, is explained in more detail, wherein a flow chart of the proposed solution is shown in **Fig.2b**.

If it is started with a wrong description of the type of fiber, the initial value of the nonlinear coefficient γ , i.e. $\gamma(0)$, has to be estimated. Based on the fact that the nonlinear fiber coefficient γ , for commonly installed fibers, varies from 0.6 1/(W*km) (in case of Large-Effective Area Pure Silica Core Fiber (LA-PSCF)), to about 2 1/(W*km) (for the case of non-zero-dispersion shift fiber), the proposed initial value for $\gamma(0)$ can be set (e.g., per default) at 1.3 1/(W*km), which may correspond to an average value for commercially available fibers. Accordingly, a different value is selected for $\gamma(1)$, wherein $\gamma(1)$ indicates the next iteration after $\gamma(0)$. The actual selected value of the nonlinear coefficient γ (represented by signal 231 in Fig.2) is forwarded to the Adaptive DBP Module 202.

After frame recovery of the incoming signal 120 processed by the carrier recovery module 105, training sequences (TS) being part of the received signal 120 are extracted and used to derive the residual nonlinear phase difference between received and (originally) transmitted symbols or sequences of symbols - see step 250 in Fig.2b. It is noted that this is also possible without any training sequence by deriving the residual nonlinear phase difference between

received symbols and respective symbols after decision,
(which is also called "blind method" or "blind receiver").

The phase difference between the two sequences is defined
5 as

$$\Delta\theta(t) = \theta(t) - \theta_{RX}(t)$$

wherein

10

- $\theta(t)$ either represents a sequence of training symbols, ($\theta(t) = \theta_{TS}(t)$) or a sequence of already decided symbols ($\theta(t) = \theta_{DEC}(t)$) and
- $\theta_{RX}(t)$ represents the received symbols.

15

Both, the use of a blind receiver (using decided symbols $\theta(t) = \theta_{DEC}(t)$) and the use of a data-aided method (using training symbols $\theta(t) = \theta_{TS}(t)$) is valid.

20 According to a further embodiment the phase difference between two symbols (or sequences of symbols) can also be determined as follows:

$$\Delta\theta(t) = |\theta(t) - \theta_{RX}(t)|$$

25

where $|\dots|$ represents the absolute value of the phase difference $\Delta\theta(t)$.

For this example a 16 QAM modulation format is applied for
30 the received signal 120. **Fig. 3** presents the respective histogram 300 of the derived phase difference $\Delta\theta(t)$ of such kind of 16 QAM modulated signal, comprising 12 peaks corresponding to the 12 phases of a 16 QAM modulated signal, whereby the value of the phase difference $\Delta\theta(t)$ at
35 the very left and right side of the histogram 300 represent the same angle. This phase information can be obtained by mathematically manipulating the phase information being

part of the received symbols (e.g., elimination of phase ambiguity).

Following the proposed method, the 4th power is applied to the incoming signal 120 before deriving the residual nonlinear phase difference at the adaptive Estimation Module 210. The respective histogram 400 of the 4th power signal is shown in **FIG.4** where only three phases of a single quadrant can be identified accordingly. This information ("spreading of received symbols"), presented in Fig.4, is the basis for calculating the nonlinear coefficient γ by deriving and evaluating a cost function as suggested - step 251 in Fib.2b.

As it can be seen by the peak in the middle of the histogram ($\Delta\theta=0$) of **Fig.4**, some phases of the received symbols are identified more frequently, because two of the symbols of the 4th-power of a 16 QAM constellation as shown in Fig.5 are corresponding to the same phase - represented by symbol 502 and 503 in Fig.5.

Based on the information available in **Fig.4**, i.e. based on the identified phase difference of the 4th-power of the incoming 16 QAM signal, the following cost function can be determined:

$$CF = [\delta_{\theta 1} + \delta_{\theta 3}] * (1/R_2) + \delta_{\theta 2} * (1/R_1 + 1/R_3)$$

wherein

- $\delta_{\theta 1}$, $\delta_{\theta 2}$, and $\delta_{\theta 3}$ are representing the standard deviation for each of the respective phase differences as shown in Fig. 4, and
- R1, R2 and R3 are representing the radii of the 16 QAM constellation as shown in FIG.5.

The cost function CF is the basis for estimating a variation $\Delta\gamma$ of gamma, which is now explained in more detail:

5 An optimized (in the purpose of improved) value of the nonlinear coefficient γ can be calculated by minimizing the cost function CF mentioned above. The algorithm for optimizing the nonlinear coefficient value γ (e.g., according to the "steepest descent algorithm", which is a
10 known optimization algorithm, "http://en.wikipedia.org/wiki/Gradient_descent") is iteratively applied and, e.g., implemented in the adaptive Estimation Module 210 as follows:

$$15 \quad \gamma(i+1) = \gamma(i) + \mu\Delta\gamma(i)$$

wherein:

- i is the index of the discrete time;
- 20 - $\gamma(i+1)$ represents the value of the nonlinear coefficient at the iteration $(i+1)$;
- $\gamma(i)$ represents the value of the nonlinear coefficient at the preceding iteration (i) ;
- μ represents a convergence factor, comprising an
25 effective fiber length L_{eff} and a channel power P .

The effective fiber length may be derived according to the following exemplary relation:

$$L_{eff} = \frac{1 - \exp(-\alpha L)}{\alpha}$$

30

wherein

α is a fiber attenuation defined in [Np/km].

The algorithm can also be applied by considering only the algebraic sign of the gradient.

Each iteration $\Delta\gamma(i)$ can be derived according to the
5 following equation:

$$\Delta\gamma(i) = \partial CF(\gamma) / \partial \gamma$$

wherein $\partial CF(\gamma) / \partial \gamma$ is a gradient of the cost function over
10 the nonlinear coefficient.

By substituting $\Delta\gamma(i)$ in the iterative optimization algorithm, the new value of the nonlinear coefficient γ can be determined according to:

15

$$\gamma(i+1) = \gamma(i) + \mu \frac{\partial CF(\gamma)}{\partial \gamma}$$

The new value of the nonlinear coefficient $\gamma(i+1)$ is forwarded to the adaptive DBP module 202, wherein the received signal 120 is processed by applying the new value
20 $\gamma(i+1)$ - step 253 in Fig. 2b.

After each iteration, the gradient of the cost function CF is evaluated with respect to the previous iteration, whereas a change of the sign of the gradient indicates an
25 end of the iteration loop, i.e. a minimum of the cost function has been reached. At this stage the iterative optimization algorithm can be stopped - step 252 in Fig. 2b.

30 **Fig.6** shows an example (calculated by simulated data) of the derived cost function CF as a function of the nonlinear coefficient γ based on a SSMF fiber with 16-QAM.

The algorithm for determining the optimized value of the
35 nonlinear coefficient γ starts by calculating two results

of the cost function CF (corresponding to two different initial values of γ).

In addition, the convergence factor μ has to be optimized
5 as well to achieve a reduction of computational time without losing quality in estimation accuracy.

In a further example shown in **Fig.7** the respective cost
function CF of an 8x82 km SSMF fiber was investigated based
10 on experimental data, considering a launch power of 3 dBm.

According to Fig.6 and 7 several important aspects of the proposed solution can be identified:

- 15 - The information being available after carrier recovery of the received signal is sufficient for determination of the optimized value of the nonlinear coefficient γ , i.e. FEC (forward error correction) based on a BER calculation can be avoided. Advantageously, the
20 convergence factor for estimating the optimum value of the nonlinear coefficient γ can be significantly accelerated.
- The cost function CF can be derived analytically wherein
25 verification of the results can be achieved by post-processing simulated and experimental data.
- The robustness of the proposed approach has been
30 verified under extreme conditions, showing that an appropriate determination of the nonlinear coefficient γ is always successful.

Fig.8 and Fig.9 show examples concerning the quality
performance of the proposed method based on a Log10(BER)
35 versus power (dBm) performance, wherein Log10(BER) is correlated with the quality of the received signal 120
after BER calculation.

Fig.8 is showing the $\text{Log}_{10}(\text{BER})$ versus power (dBm) performance for simulated data propagated over a 8x82km LA-PSCF. The first curve (FDE) is showing the alignment of the signal-quality dependent from the power injected into the fiber by compensating only linear impairments using a Frequency Domain Equalizer (FDE). The second curve ($0.6=\gamma_{\text{BP}}$) is showing the respective quality alignment by applying a Digital Back Propagation based on a fixed nonlinear coefficient $\gamma = 0.6 \text{ 1}/(\text{W}\cdot\text{km})$ which is assumed to be the correct value for the fiber. The third curve ($1=\gamma_{\text{BP}}$) is showing the respective quality alignment by applying a Digital Back Propagation based on a wrong nonlinear coefficient value $\gamma = 1 \text{ 1}/(\text{W}\cdot\text{km})$. The fourth curve (A_BP with initial $\gamma=1$) is showing the respective quality alignment by applying an adaptive Digital Back Propagation according to the proposed solution by starting with a (wrong) initial value of the nonlinear coefficient $\gamma = 1$. As there is only a small difference between the alignment of the second and fourth curve it can be verified, that the proposed method is working correctly, i.e. the derived optimized value of the nonlinear coefficient γ after termination of the optimization algorithm according to the proposed method is exactly the same or nearly the same value like the nonlinear coefficient value γ of the real fiber.

Fig.9 is showing the $\text{Log}_{10}(\text{BER})$ versus power (dBm) performance for experimental data propagated over 8x82 km of SSMF. Again, the first curve (FDE) is showing the alignment of the quality dependent from the power injected into the fiber by only compensating linear impairments using a Frequency Domain Equalizer (FDE). The second curve ($0.6=\gamma_{\text{BP}}$) is showing the respective quality alignment by applying a Digital Back Propagation based on a fixed nonlinear coefficient $\gamma = 0,6 \text{ 1}/(\text{W}\cdot\text{km})$ which is the correct value according to information of the supplier of the

fiber. The third curve ($1,3=\gamma_{BP}$) is showing the respective quality alignment by applying a Digital Back Propagation based on a wrong nonlinear coefficient value $\gamma = 1,3$ $1/(W \cdot km)$. The fourth curve (A_BP with initial $\gamma=1,3$) is again showing the respective quality alignment by applying an adaptive Digital Back Propagation according to the proposed solution by starting with a (wrong) initial value of the nonlinear coefficient $\gamma = 1,3$. Again only small differences can be identified between the second and fourth curve, which means that the proposed adaptive Back Propagation algorithm is working correctly even by selecting a wrong initial value of the nonlinear coefficient γ .

It should be noted, that the aforementioned cost function CF, determined exemplarily for processing a 16 QAM modulated signal, is one possible embodiment applying the proposed solution. The proposed solution can be applied for all kinds of modulation formats.

The aforementioned cost function can be generalized as follows:

$$CF_{gen} = \sum_{k \in K} \left[(\delta_{upper,k} + \delta_{lower,k}) \cdot \frac{1}{R_k} \right] + \delta_{center} \cdot \sum_{i \in I} \frac{1}{R_i}$$

with $k \in K; i \in I$

wherein

- CF_{gen} is a general cost function
- $\delta_{upper,k}$ represents a standard deviation for each of the phase differences θ_{upper} higher than a central phase θ_{center} per radius R_k
- $\delta_{lower,k}$ represents a standard deviation for each of the phase differences θ_{lower} lower than the central phase $\theta_{central}$ per radius R_k

- $\Theta\delta_{center}$ represents a central phase.
- I represents a set of distinct radii of the signal constellation
- K represents a set of distinct phase angles of the histogram of the signal constellation after a M-th power operation

Adapting the general cost function CF_{gen} for receiving of the 16 QAM modulated signal (as already being part of the exemplary description of the proposed solution), may result to the following cost function CF_{16} :

$$CF_{16} = \sum_{k \in K}^{K_{max}} (\delta_{upper} + \delta_{lower}) \cdot \frac{1}{R_2} + \delta_{center} \cdot \left(\frac{1}{R_1} + \frac{1}{R_3} \right)$$

with $k \in [2]; i \in [1,3]$

Fig. 10 shows the corresponding 16 QAM constellation diagram applied to the 4th power.

Hereinafter, examples are provided, adapting the general cost function CF_{gen} for processing different modulation formats of the received signal.

Adapting the general cost function CF_{gen} for receiving of a 32 QAM modulated signal:

$$CF_{32} = \sum_{k \in K} \left[(\delta_{upper,k} + \delta_{lower,k}) \cdot \frac{1}{R_k} \right] + \delta_{center} \cdot \sum_{i \in I} \frac{1}{R_i}$$

with $k \in [2,4,5]; i \in [1,3]$

Fig.11 shows the corresponding 32 QAM constellation diagram applied to the 4th power.

Adapting the general cost function CF_{gen} for receiving of a 64 QAM modulated signal:

$$CF_{64} = \sum_{k \in K} \left[(\delta_{upper,k} + \delta_{lower,k}) \cdot \frac{1}{R_k} \right] + \delta_{center} \cdot \sum_{i \in I} \frac{1}{R_i}$$

with $k \in [2, 4, 5, 6, 7, 8]$; $i \in [1, 3, 6, 9]$

5 **Fig.12** shows the corresponding 64 QAM constellation diagram to the 4th power.

For receipt of a M-PSK modulated signal, the following cost function can be determined:

10

$$CF_{M-PSK} = \frac{\delta}{R}$$

with $k = 0$; $i = 1$

Fig.13 shows the corresponding M-PSK constellation diagram to the 4th power.

15 In real DWDM systems details on the transmission link are not or only partially available. Even, if details were available, with the upcoming automatically switched optical networks (ASON / GMPLS) an exact knowledge of the link description would not be available any more, particularly
 20 after protection switching or even active traffic routing. The proposed solution for adaptive Digital Back Propagation is capable of a suitable set of parameters for a DBP implementation after a very short initialization cycle.

25 As a further advantage, no significant changes in the optical receiver are necessary for implementing the proposed solution. The coding of the optimization algorithm can be implemented in a DSP (Digital Signal Processor).

30 The proposed approach can be implemented in various optical transmission systems using coherent detection, including

single carrier and multi carrier, single mode and multi mode.

List of Abbreviations:

	DBP	Digital Back-Propagation
	DEC	Decision
5	DSP	Digital Signal Processor
	DWDM	Dense Wavelength Division Multiplex
	BER	Bit Error Rate
	CD	Chromatic Dispersion
	CF	Cost Function
10	CPR	Carrier Phase Recovery
	CR	Clock Recovery
	DSP	Digital Signal Processing
	DM	Dispersion Managed
	FDE	Frequency-Domain Equalizer
15	NDM	Non-Dispersion Managed
	NLPN	Nonlinear Phase Noise
	PMD	Polarization Mode Dispersion
	RX	Receive
	SPM	Self Phase Modulation
20	TDE	Time-Domain Equalizer
	TS	Training Sequence
	XPM	Cross Phase Modulation

Claims:

1. A method for reducing optical transmission impairments, particularly nonlinear effects, of at least one link,
5 comprising the following steps:
 - a) extracting a phase information ($\Delta\theta$) from an optical signal (120) received via the at least one link,
 - b) determining a nonlinear coefficient (γ), associated
10 with the at least one link, based on the phase information ($\Delta\theta$),
 - c) applying a control mechanism (202) using the nonlinear coefficient (γ).
- 15 2. The method according to claim 1, repeating the steps a) to c) until the nonlinear coefficient value (γ) reaches or exceeds a value.
3. The method according to claim 1 or 2, wherein the
20 control mechanism (202) comprises a Digital Backward Propagation algorithm.
4. The method according to any of the preceding claims, wherein the phase information ($\Delta\theta$) is extracted after
25 a carrier recovery (105) of the received optical signal (102).
5. The method according to any of the preceding claims, wherein
30
 - a cost function (CF) is derived based on the extracted phase information ($\Delta\theta$), and
 - an optimization algorithm is applied in connection with that cost function (CF) to determine the nonlinear coefficient (γ).
- 35 6. The method according to any of the preceding claims, wherein

- the extracted phase information comprises a spreading of receiving symbols (501...504) being part of that received optical signal (102), and
 - the determination of the nonlinear coefficient (γ) is such that a reduced spreading of the receiving symbols (501...504) is achieved.
- 5
7. The method according to claim 6, wherein the respective spreading of the received symbols (501...504) comprises respective phase differences ($\Delta\theta$) between the received symbols (θ_{TS} , θ_{DEC}) and respective transmitted symbols (θ_{RX}) which are derived either with or without a training sequence.
- 10
8. The method according to claim 7, wherein
- the received optical signal (102) is a coherent signal based on a 16 QAM modulation,
 - the 4th power is applied to the received optical signal,
 - the respective phase differences ($\Delta\theta$) are derived from a 4th power signal,
 - the cost function (CF), based on those derived phase differences ($\Delta\theta$), is defined as
- 15
- $$CF = [\delta_{\theta 1} + \delta_{\theta 3}] * (1/R_2) + \delta_{\theta 2} * (1/R_1 + 1/R_3)$$
- 20
- 25
- wherein
- $\delta_{\theta 1}$, $\delta_{\theta 2}$, and $\delta_{\theta 3}$ are representing the standard deviation for each of the respective phase differences, and
 - R1, R2 and R3 are representing the radii of the 16 QAM constellation.
- 30
9. The method according to one of the preceding claims 5 to 8, wherein the optimization algorithm is based on the steepest descent algorithm.
- 35

10. The method according to claim 9, wherein the steepest descent algorithm is defined as

5
$$\gamma(i + 1) = \gamma(i) + \mu \Delta\gamma(i)$$

wherein

- i is the index of the discrete time
- 10 - $\gamma(i+1)$ is representing the value of the nonlinear coefficient at iteration (i+1)
- $\gamma(i)$ is representing the value of the nonlinear coefficient at the preceding iteration step (i)
- μ is representing the convergence factor,
15 comprising an effective fiber length L_{eff} and a channel power P.
- $\Delta\gamma(i) = \partial\text{CF}(\gamma) / \partial\gamma$

11. The method according to claim 9 or 10, wherein
- 20 - the optimization algorithm starts by calculating two values of the cost function corresponding to two different values of the nonlinear coefficient (γ), and
 - the first starting value of the nonlinear
25 coefficient (γ) is represented by an selected initial value.

12. The method according to any of the preceding claims, wherein
- 30 - the nonlinear coefficient (γ) is refined as a n-dimensional nonlinear coefficient, representing n single links,
 - the n-dimensional nonlinear coefficient is
35 determined by a n-dimensional calculation.

13. A device comprising
- a control mechanism for reducing optical transmission impairments, particularly nonlinear effects, of at least one single link which can be connected to the device and
 - a processor unit that is arranged such that the following steps can be executed:
 - a) extracting a phase information ($\Delta\theta$) from an optical signal (120) received via that at least one link,
 - b) determining a nonlinear coefficient (γ), associated with the at least one link, based on the phase information ($\Delta\theta$),
 - c) applying the control mechanism (202) using the nonlinear coefficient (γ).
14. The device according to claim 13, wherein the processor unit is arranged such that the steps a) to c) can be repeated until the nonlinear coefficient value (γ) reaches or exceeds a value.
15. The device according to claim 13 or 14, wherein said device is a communication device, in particular a or being associated with a receiver for optical signals.
16. Communication system comprising the device according to one of the preceding claims 13 to 15.

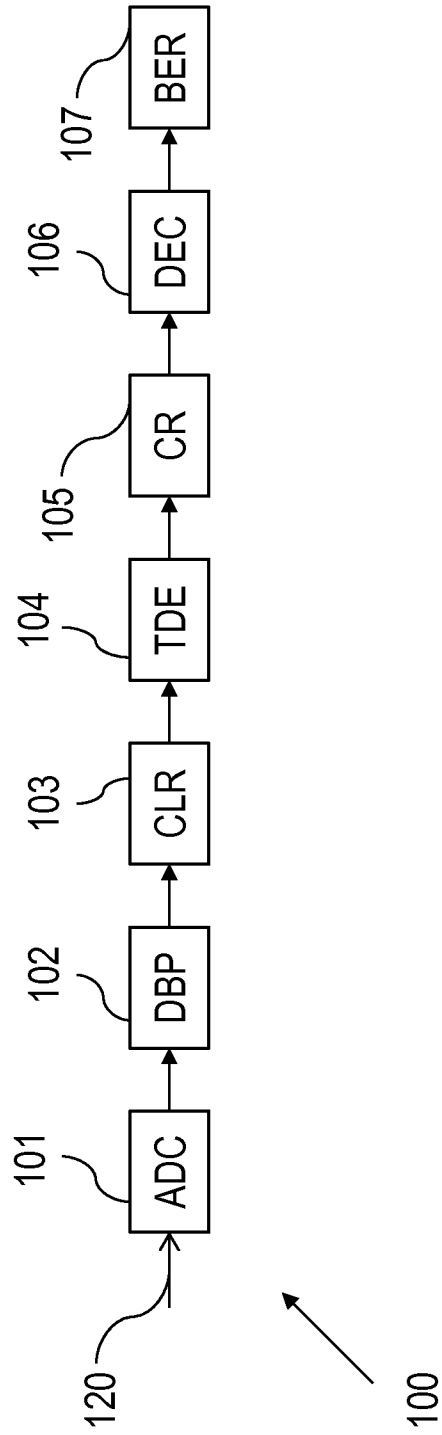


Fig.1

Fig.2a

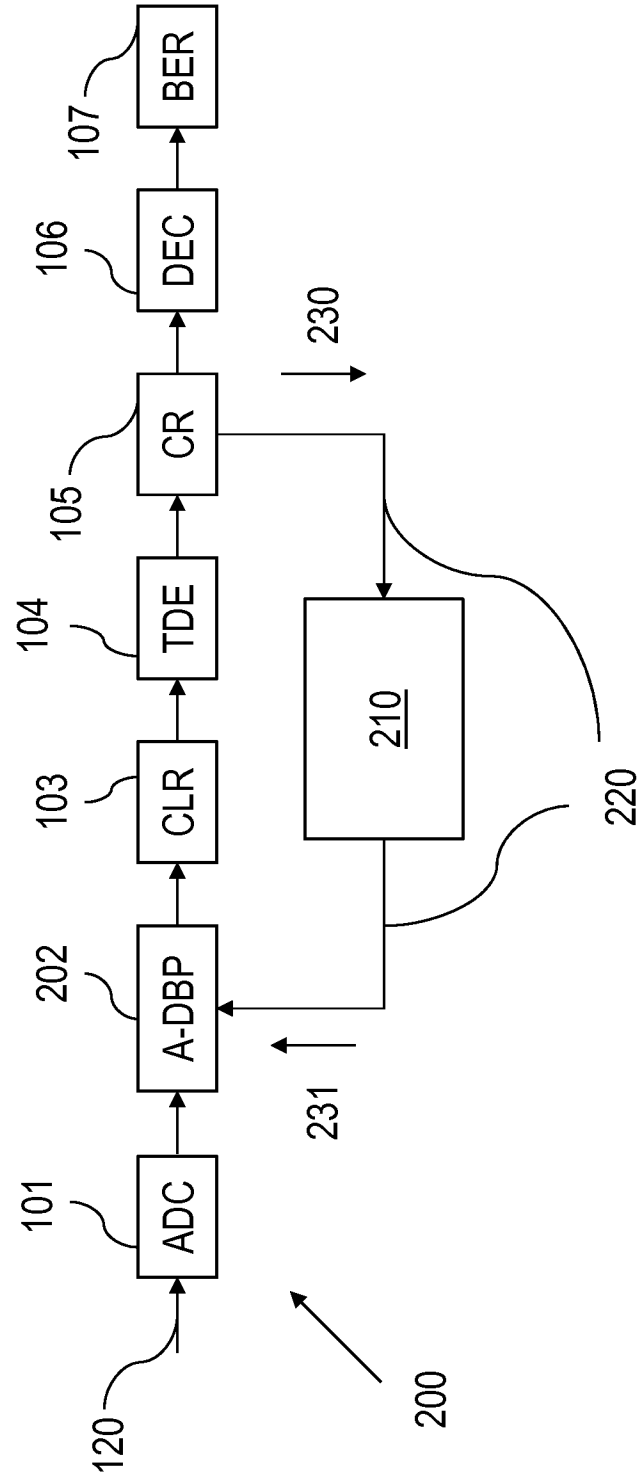
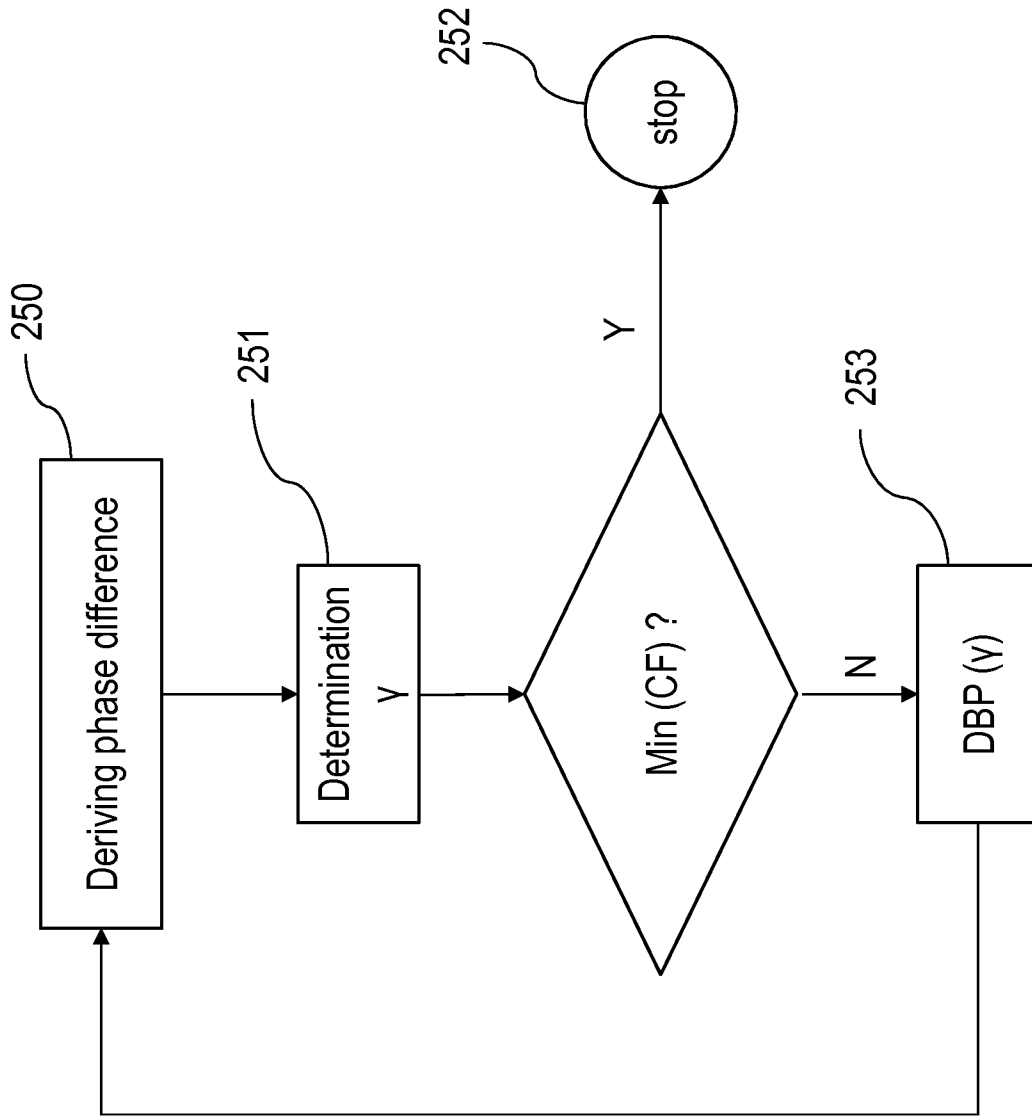


Fig.2b



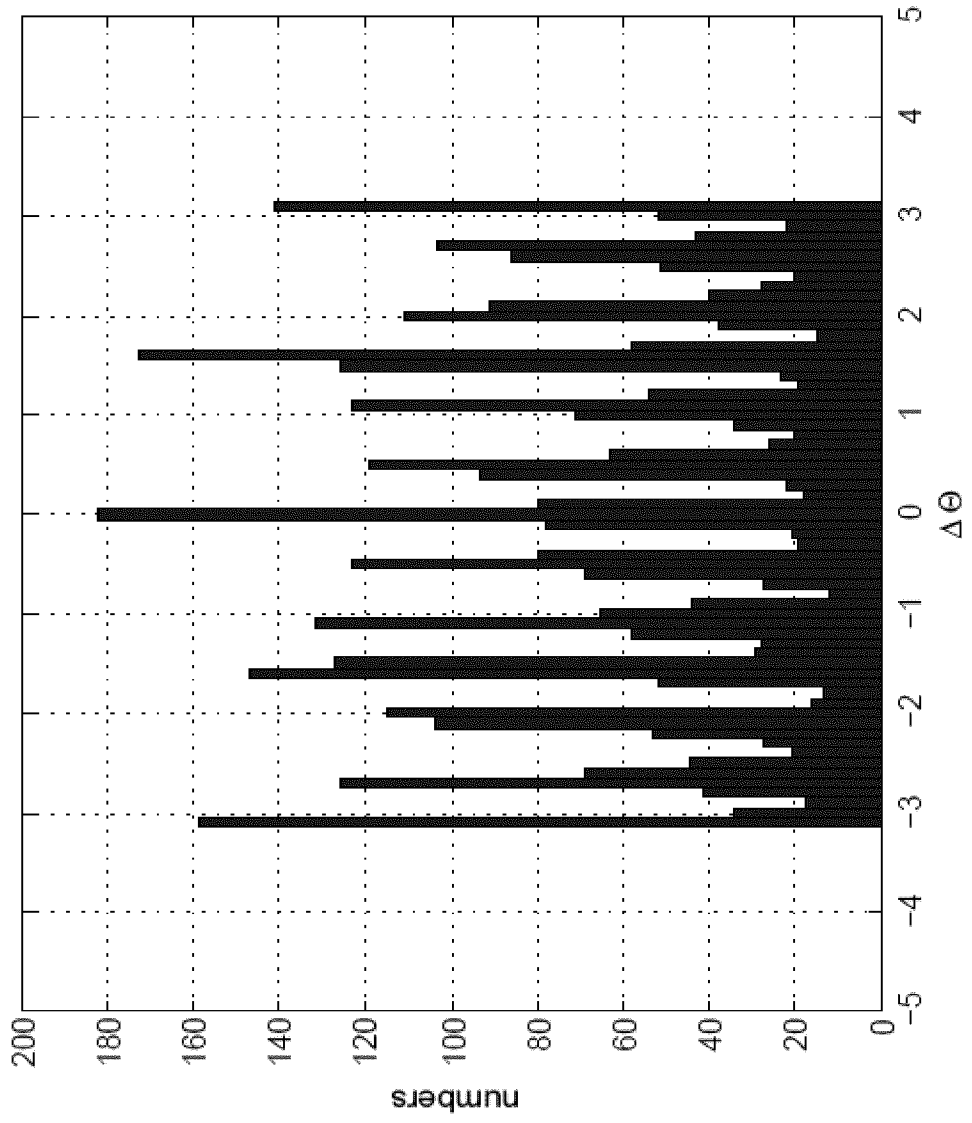


Fig.3

300



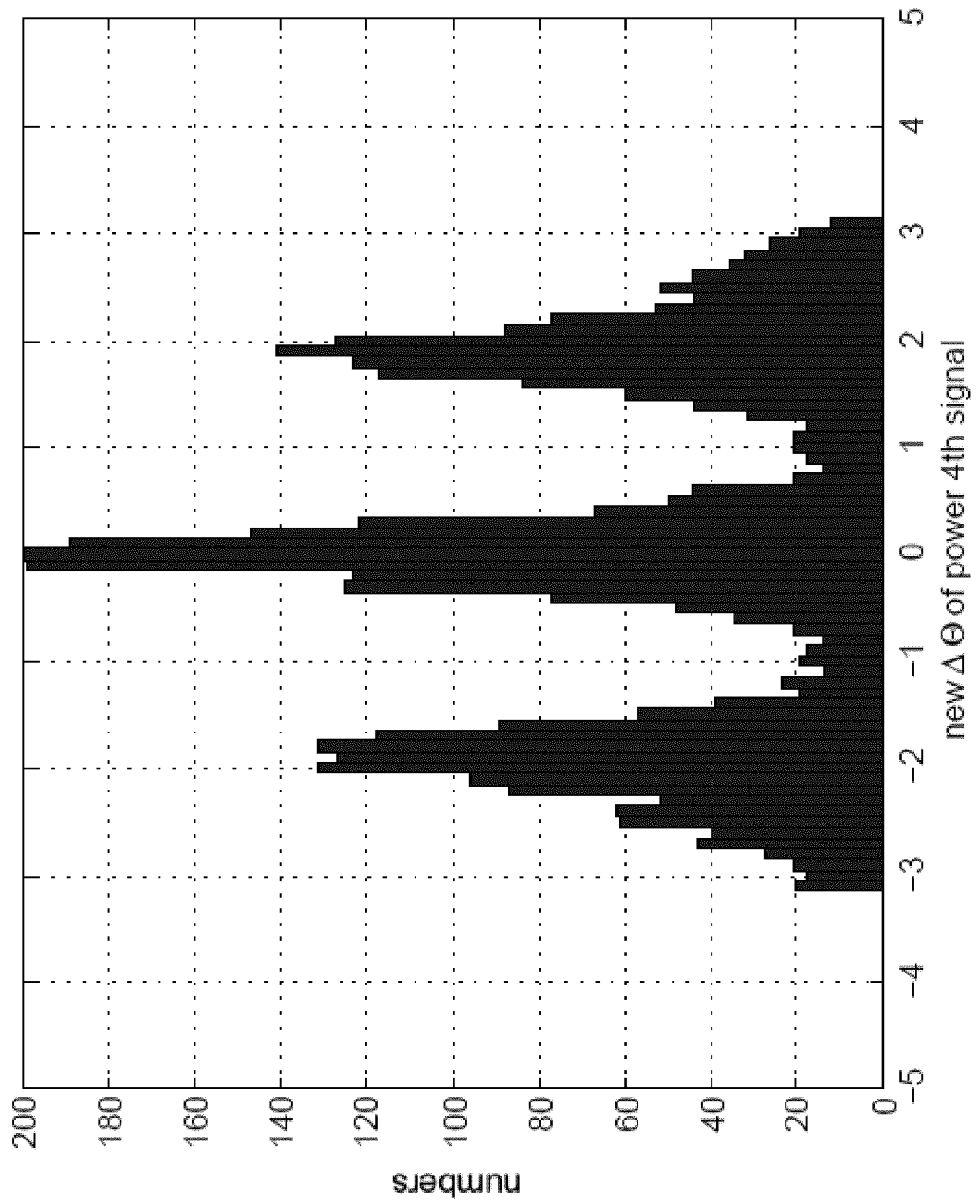


Fig.4

400



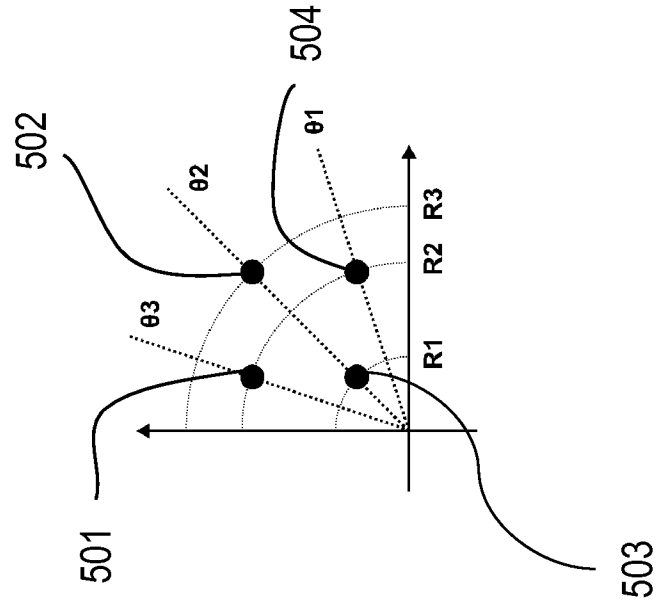
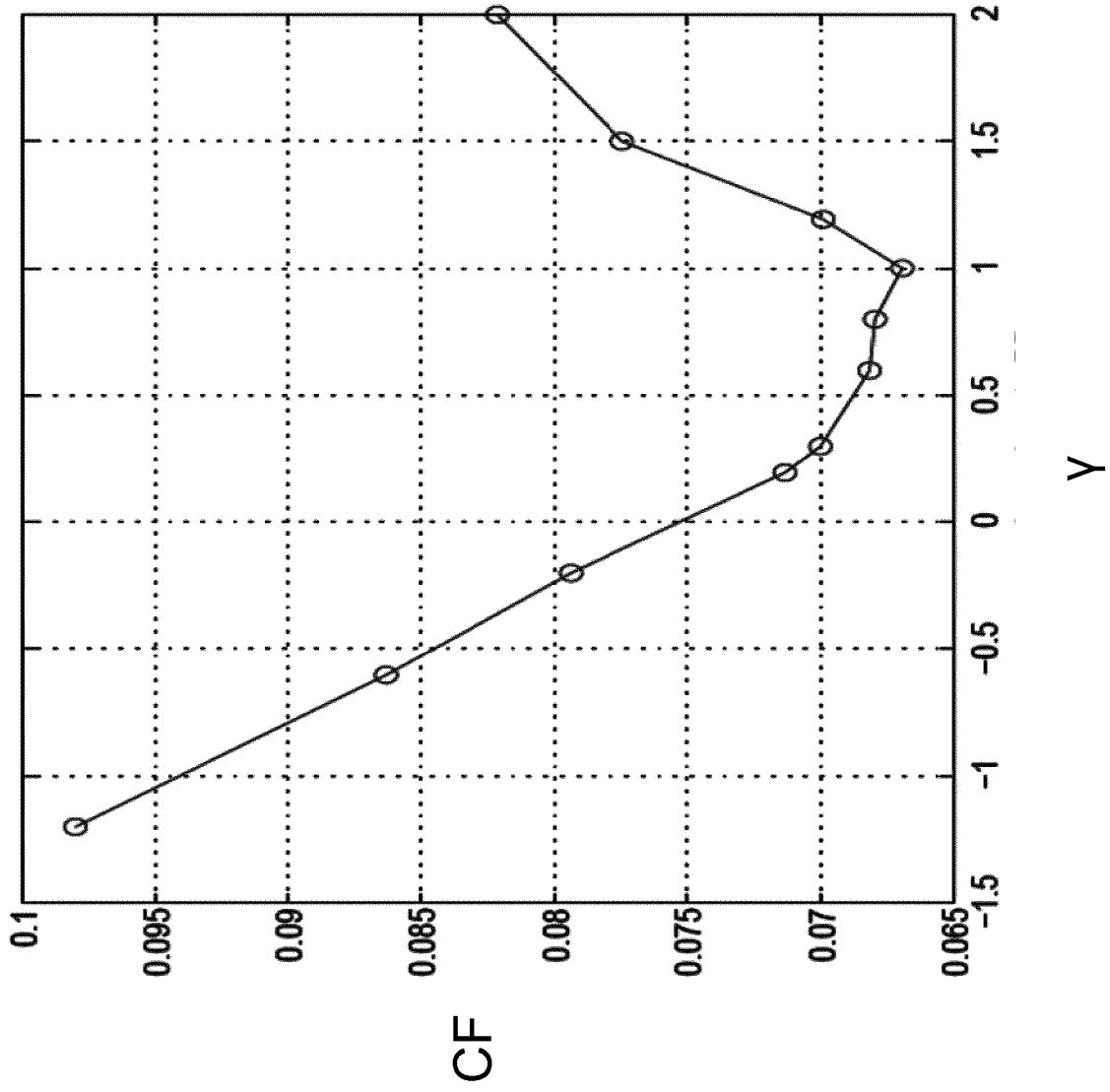


Fig.5

Fig.6



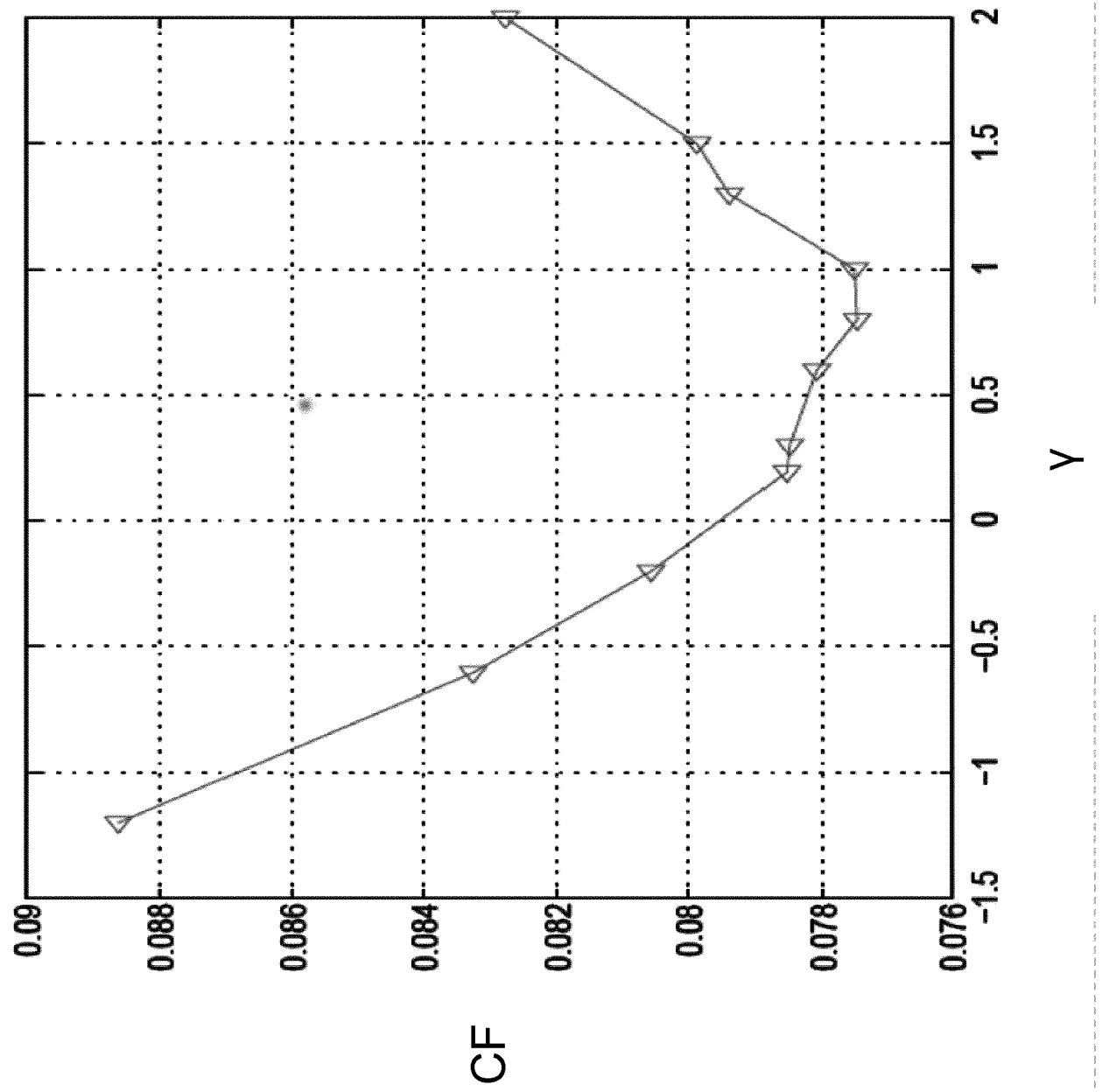


Fig.7

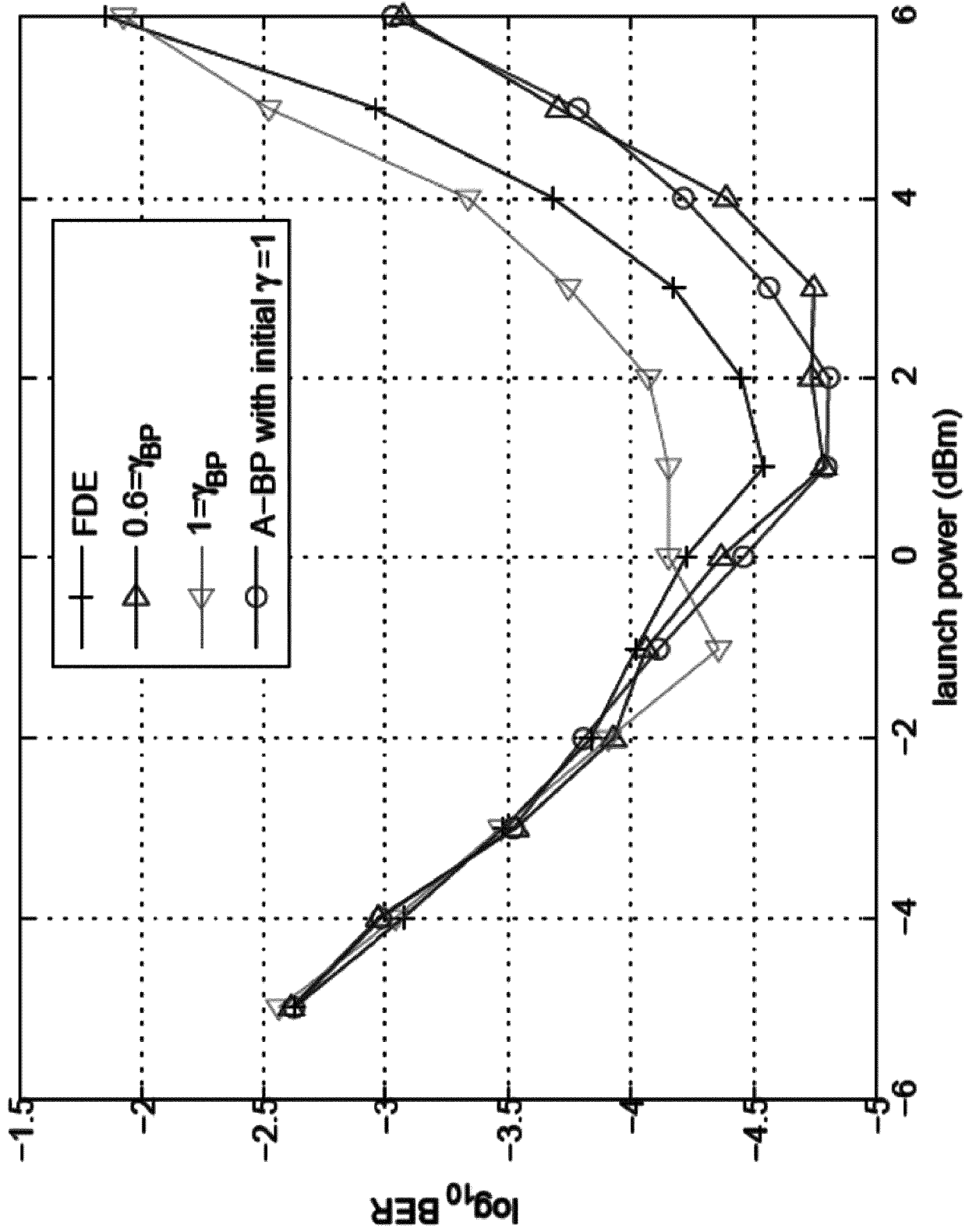


Fig.8

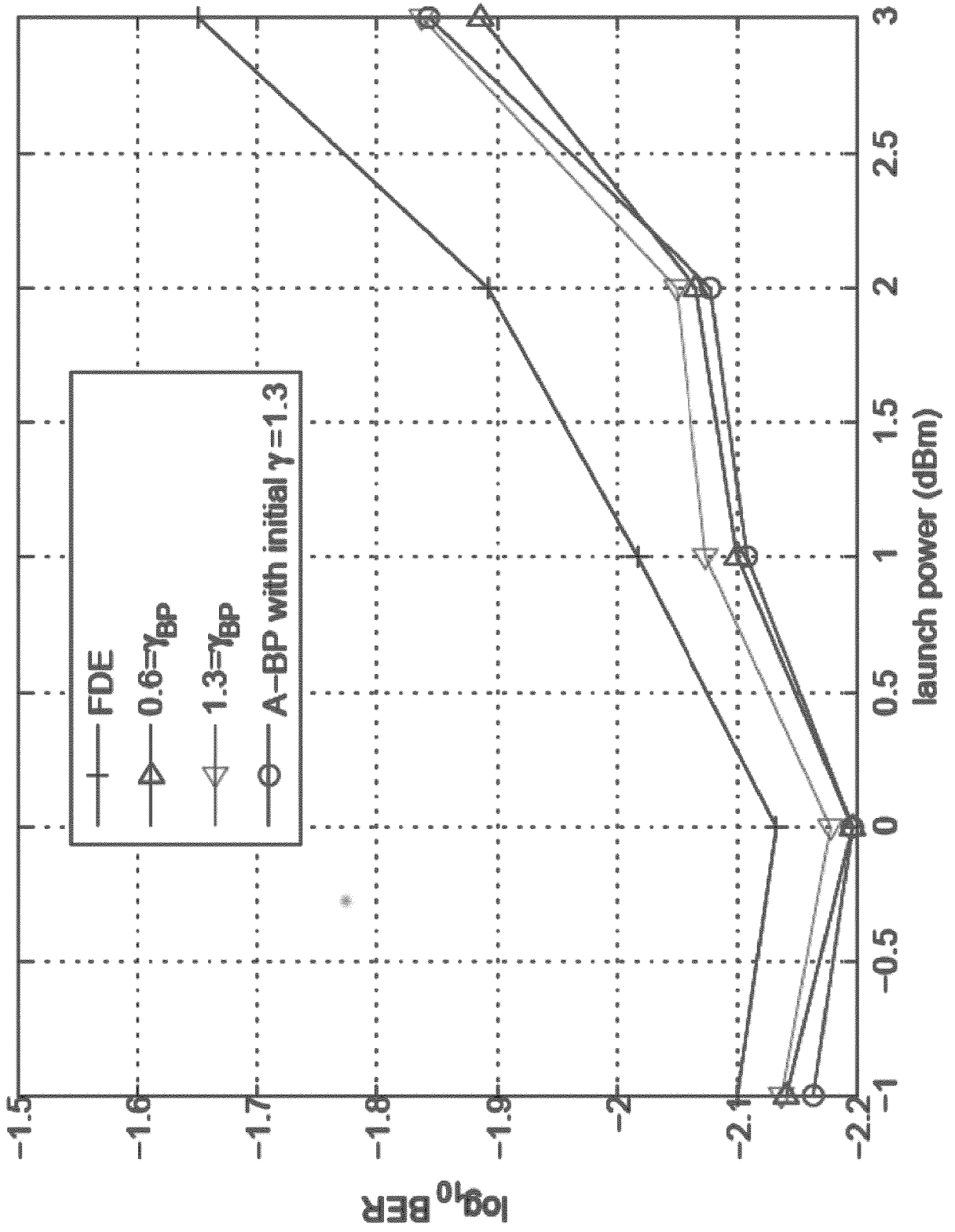


Fig.9

16 QAM

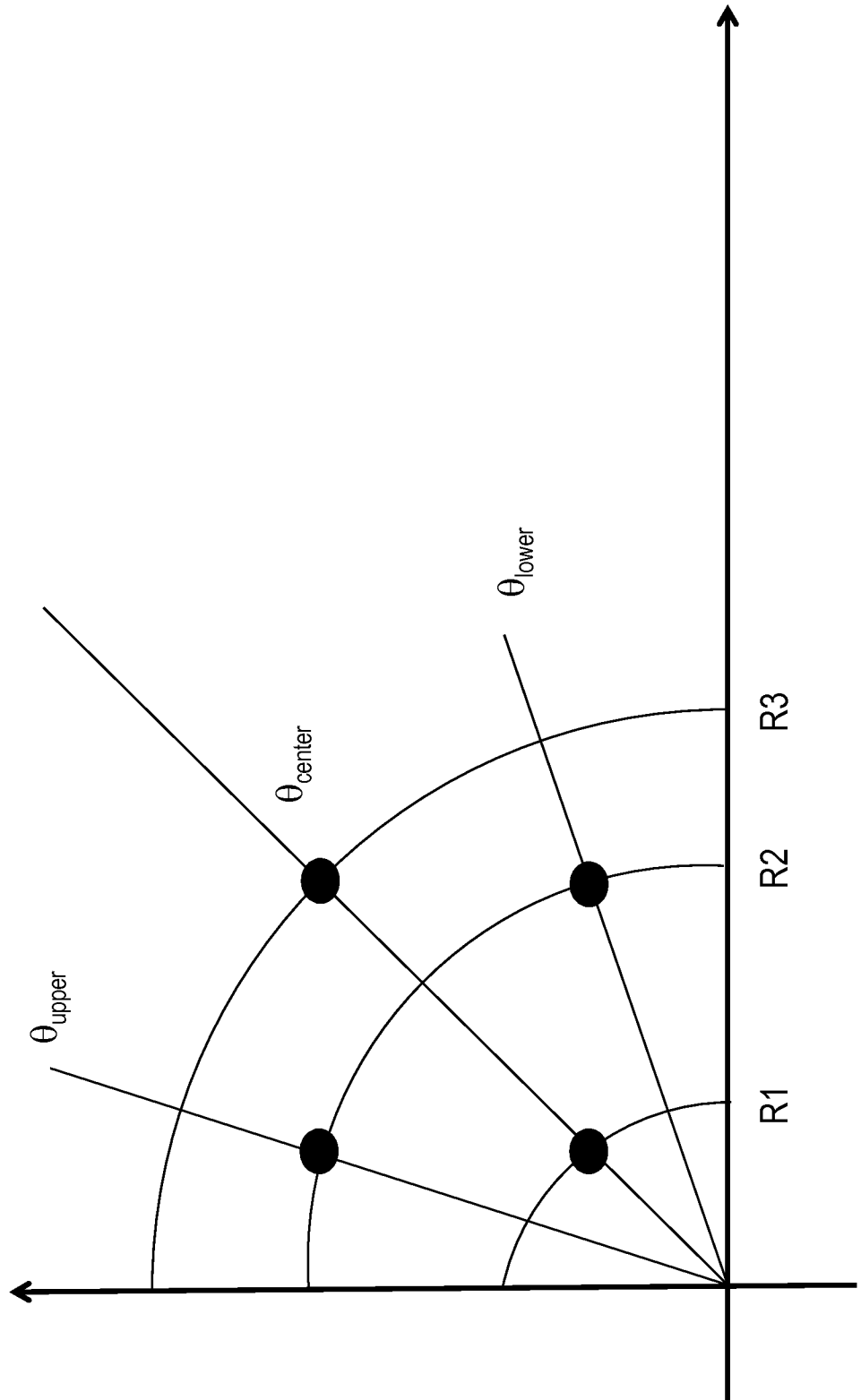
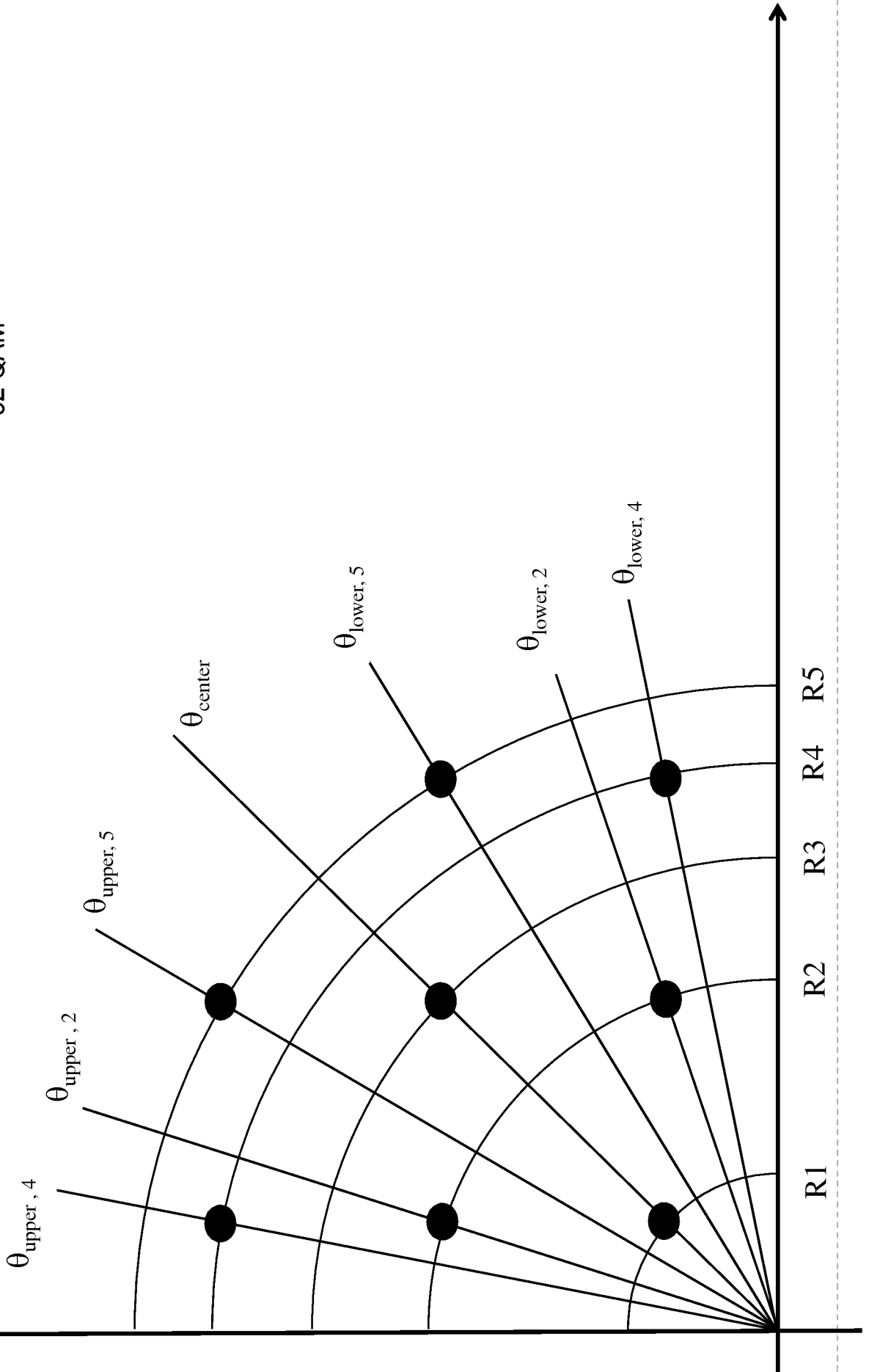


Fig.10

Fig.11

32 QAM



64 QAM

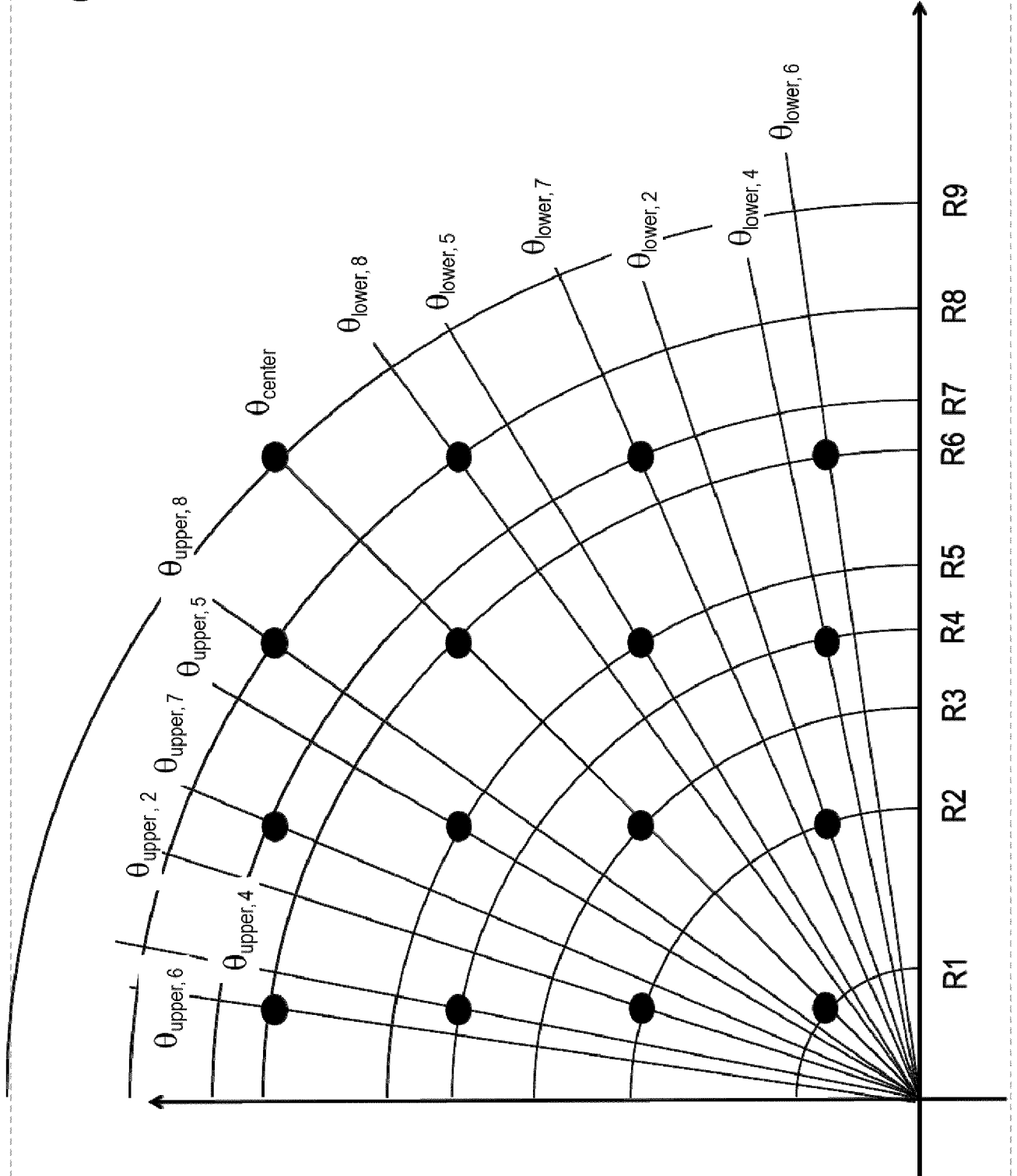


Fig.12

M-PSK

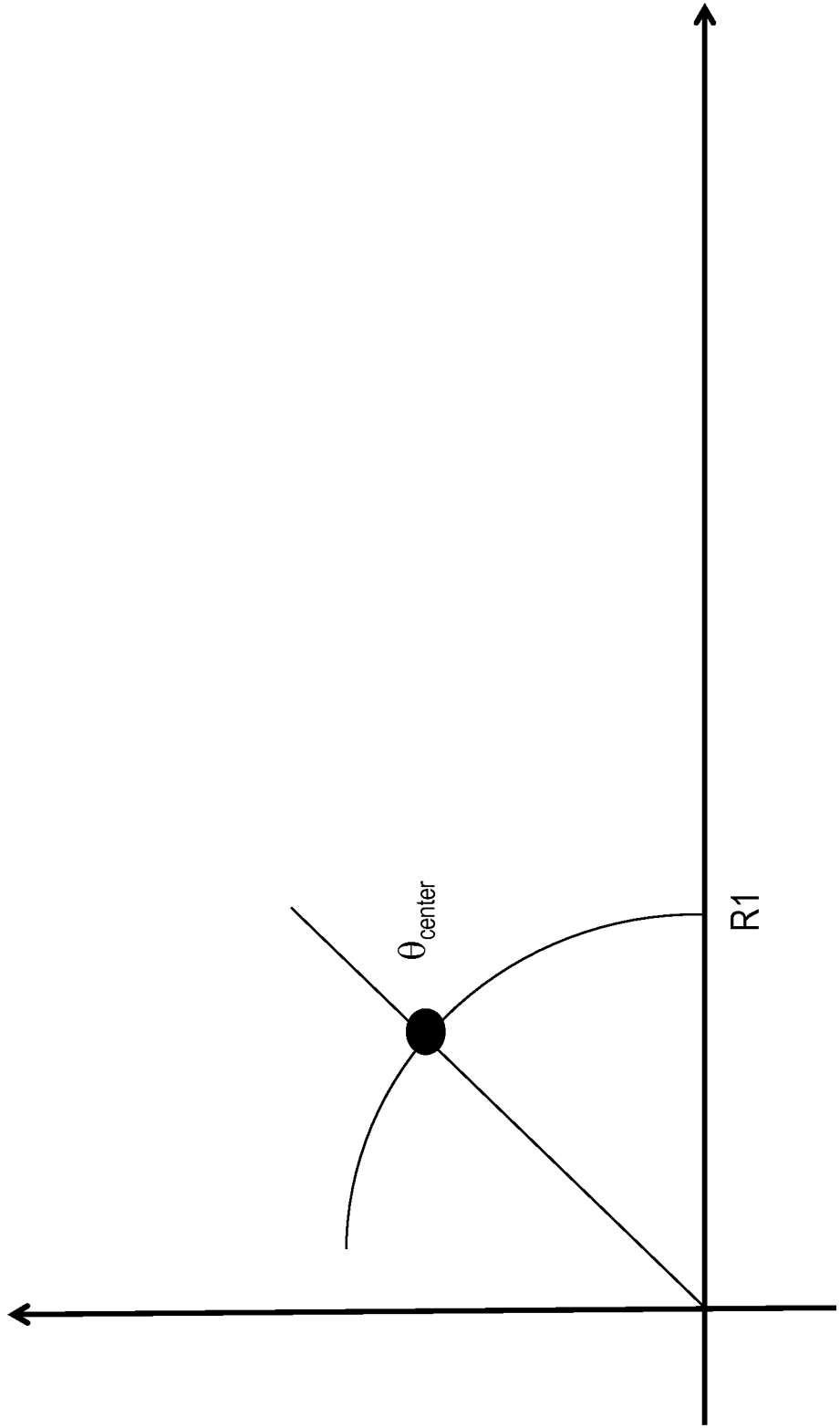


Fig.13

INTERNATIONAL SEARCH REPORT

International application No PCT/EP2014/059654

A. CLASSIFICATION OF SUBJECT MATTER INV. H04B10/2543 ADD.		
According to International Patent Classification (IPC) or to both national classification and IPC		
B. FIELDS SEARCHED		
Minimum documentation searched (classification system followed by classification symbols) H04B		
Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched		
Electronic data base consulted during the international search (name of data base and, where practicable, search terms used) EPO-Internal, INSPEC, WPI Data		
C. DOCUMENTS CONSIDERED TO BE RELEVANT		
Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
X	ASIF ET AL.: "Optimized digital backward propagation for phase modulated signals in mixed-optical fiber transmission links", OPTICS EXPRESS, vol. 18, no. 22, 25 October 2010 (2010-10-25), pages 22796-22807, XP002715061, cited in the application	1-4, 12-16
A	the whole document ----- -/--	5-11
<input checked="" type="checkbox"/> Further documents are listed in the continuation of Box C. <input type="checkbox"/> See patent family annex.		
* Special categories of cited documents :		
"A" document defining the general state of the art which is not considered to be of particular relevance "E" earlier application or patent but published on or after the international filing date "L" document which may throw doubts on priority claim(s) or which is cited to establish the publication date of another citation or other special reason (as specified) "O" document referring to an oral disclosure, use, exhibition or other means "P" document published prior to the international filing date but later than the priority date claimed	"T" later document published after the international filing date or priority date and not in conflict with the application but cited to understand the principle or theory underlying the invention "X" document of particular relevance; the claimed invention cannot be considered novel or cannot be considered to involve an inventive step when the document is taken alone "Y" document of particular relevance; the claimed invention cannot be considered to involve an inventive step when the document is combined with one or more other such documents, such combination being obvious to a person skilled in the art "&" document member of the same patent family	
Date of the actual completion of the international search	Date of mailing of the international search report	
7 August 2014	18/08/2014	
Name and mailing address of the ISA/ European Patent Office, P.B. 5818 Patentlaan 2 NL - 2280 HV Rijswijk Tel. (+31-70) 340-2040, Fax: (+31-70) 340-3016	Authorized officer Petitit, Nicolas	

INTERNATIONAL SEARCH REPORT

International application No PCT/EP2014/059654

C(Continuation). DOCUMENTS CONSIDERED TO BE RELEVANT		
Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	<p>GUIOMAR F P ET AL: "Optimizing the nonlinear operator in backward propagation", EUROCON - INTERNATIONAL CONFERENCE ON COMPUTER AS A TOOL (EUROCON), 2011 IEEE, 27-29 APRIL 2011, LISBON PORTUGAL, IEEE, PISCATAWAY, NJ, 27 April 2011 (2011-04-27), pages 1-4, XP031949634, DOI: 10.1109/EUROCON.2011.5929356 ISBN: 978-1-4244-7486-8 the whole document</p> <p align="center">-----</p>	1-16
A	<p>TAKAHITO TANIMURA ET AL: "Semi-blind nonlinear equalization in coherent multi-span transmission system with inhomogeneous span parameters", OPTICAL FIBER COMMUNICATION (OFC), COLLOCATED NATIONAL FIBER OPTIC ENGINEERS CONFERENCE, 2010 CONFERENCE ON (OFC/NFOEC), IEEE, PISCATAWAY, NJ, USA, 21 March 2010 (2010-03-21), pages 1-3, XP031676785, cited in the application the whole document</p> <p align="center">-----</p>	1-16