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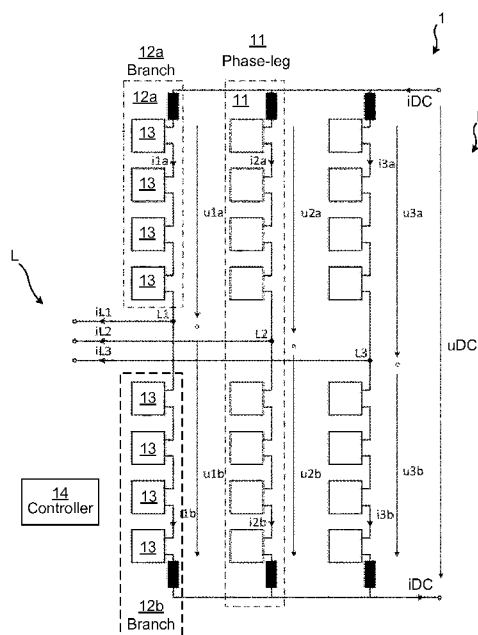


Fig. 1

(57) Abstract: The present disclosure relates to a method of controlling a DC-to-AC Modular Multilevel Converter (MMC) (1) having a three-phase AC side connected to a three-phase AC network L and having a DC side connected to a DC network R. The MMC has a double-star topology with a plurality of phase-legs (11). Each phase-leg has a first branch (12a) and a second branch (12b). Each of the first and second branches comprises a plurality of series connected converter cells (13). The method comprises obtaining an Optimized Pulse Pattern (OPP) for the MMC. The method also comprises adapting the OPP to the MMC by means of closed-loop pulse pattern control. The method also comprises, based on the adapted OPP, sending firing signals to the plurality of cells of each branch.

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CONTROL OF DC-TO-AC MODULAR MULTILEVEL CONVERTER

TECHNICAL FIELD

The present disclosure relates to a method of controlling a DC-to-AC (DC/AC) Modular Multilevel Converter (MMC).

5 BACKGROUND

An MMC is a power converter comprising series-connected cells (also known as modules or submodules), forming what is called a converter branch (also known as arm). These branches can be configured in several manners leading to dedicated converter topologies. Depending on whether these branches
10 need to provide only positive or also negative voltages, the cell can be implemented by means of a half-bridge (unipolar) or a full-bridge (also called bipolar or H-bridge) cell, respectively. A Direct Current (DC)-to-three-phase Alternating Current (AC) MMC structure in double-star configuration may be used for interconnection of a three-phase utility grid, e.g., 50 Hz, with a DC
15 grid, e.g. a microgrid with Distributed Generators (DG) such as in the form of photovoltaic power plants or wind turbines. Alternative applications include variable speed drives and battery energy storage systems (BESS).

SUMMARY

The present invention relates especially to a problem of medium voltage DC-
20 to-AC MMC in double-star configuration which may operate with a relatively low number of cells and low switching frequencies, e.g., close to and including the fundamental frequency of the AC network. In such cases, the inherent advantages of double-star converters, such as superior harmonic performance as well as high current control bandwidth capabilities may be
25 reduced.

In addition, conventional modulation methods such as Carrier-Based Pulse Width Modulation (CB-PWM) tend to perform poorly when operating at such low switching frequencies. In this case, it has been realized that use of programmed modulation methods such as optimized pulse patterns (OPPs)
30 are preferred, since they allow for an active shaping of the harmonic

spectrum. However, OPPs may not easily be applied to an MMC without the use of a sophisticated controller, mainly due to the presence of significant disturbances caused by the intrinsic cell capacitor voltage ripple. The latter prevents operation of the offline pre-calculated pulse pattern using a classic
5 PI controller, which assumes that the current ripple is zero at the regularly spaced sampling instants.

In accordance with the present invention, a closed-loop pulse pattern control concept is used, e.g. of the type which may be referred to as Model Predictive Pulse Pattern Control (MP3C). Such a closed-loop pulse pattern control may
10 be combined with the use of a circulating current controller, e.g. a dead-beat circulating current controller (DBC3). It will be shown that this concept can be interfaced in a very straightforward manner to the upper layer voltage balancing control scheme of an MMC.

According to an aspect of the present invention, there is provided a method of
15 controlling a DC-to-AC MMC having a three-phase AC side connected to a three-phase AC network and having a DC side connected to a DC network. The MMC has a double-star topology with a plurality of phase-legs. Each phase-leg has a first branch and a second branch. Each of the first and second branches comprises a plurality of series connected converter cells. The
20 method comprises obtaining an OPP for the MMC. The method also comprises adapting the OPP to the MMC by means of closed-loop pulse pattern control. The method also comprises, based on the adapted OPP, sending firing signals to the plurality of cells of each branch.

According to another aspect of the present invention, there is provided a
25 computer program product comprising computer-executable components for causing a controller to perform the method of any preceding claim when the computer-executable components are run on processing circuitry comprised in the controller.

According to another aspect of the present invention, there is provided a
30 controller configured for controlling a power converter. The controller

comprises processing circuitry, and storage storing instructions executable by said processing circuitry whereby said controller is operative to obtain an OPP for a DC-to-AC MMC having a three-phase AC side connected to a three-phase AC network and having a DC side connected to a DC network, wherein
5 the MMC has a double-star topology with a plurality of phase-legs, each phase-leg having a first branch and a second branch, each of the first and second branches comprising a plurality of series connected converter cells. The controller is also operative to adapt the OPP to the MMC by means of closed-loop pulse pattern control. The controller is also operative to, based on
10 the adapted OPP, send firing signals to the plurality of cells of each branch.

By means of the closed-loop pulse pattern control, the pre-calculated OPP can be adapted for the MMC to reduce influence of disturbances e.g. due to capacitor voltage ripples of the capacitors of each converter cell.

It is to be noted that any feature of any of the aspects may be applied to any
15 other aspect, wherever appropriate. Likewise, any advantage of any of the aspects may apply to any of the other aspects. Other objectives, features and advantages of the enclosed embodiments will be apparent from the following detailed disclosure, from the attached dependent claims as well as from the drawings.

20 Generally, all terms used in the claims are to be interpreted according to their ordinary meaning in the technical field, unless explicitly defined otherwise herein. All references to "a/an/the element, apparatus, component, means, step, etc." are to be interpreted openly as referring to at least one instance of the element, apparatus, component, means, step, etc., unless explicitly stated
25 otherwise. The steps of any method disclosed herein do not have to be performed in the exact order disclosed, unless explicitly stated. The use of "first", "second" etc. for different features/components of the present disclosure are only intended to distinguish the features/components from other similar features/components and not to impart any order or hierarchy
30 to the features/components.

BRIEF DESCRIPTION OF THE DRAWINGS

Embodiments will be described, by way of example, with reference to the accompanying drawings, in which:

5 Fig 1 is a schematic block diagram of an embodiment of an MMC in double-star configuration, in accordance with the present invention.

Fig 2 is a schematic diagram of an embodiment of a bipolar converter cell, in accordance with the present invention.

Fig 3 is a schematic functional block diagram of an embodiment of a converter controller, in accordance with the present invention.

10 Fig 4a is a schematic illustration of an embodiment of $N+1$ modulation, where voltage is on the vertical axis and time on the horizontal axis.

Fig 4b is a schematic illustration of an embodiment of $2N+1$ modulation, where voltage is on the vertical axis and time on the horizontal axis.

15 Fig 5a is a schematic functional block diagram of an embodiment of a converter controller including DBC3, in accordance with the present invention.

Fig 5b is a schematic functional block diagram of an embodiment of a converter controller including hysteresis circulating current control, in accordance with the present invention.

20 Fig 6 is a schematic flow chart of an embodiment of the method of the present invention.

DETAILED DESCRIPTION

Embodiments will now be described more fully hereinafter with reference to the accompanying drawings, in which certain embodiments are shown.

25 However, other embodiments in many different forms are possible within the scope of the present disclosure. Rather, the following embodiments are provided by way of example so that this disclosure will be thorough and

complete, and will fully convey the scope of the disclosure to those skilled in the art. Like numbers refer to like elements throughout the description.

Figure 1 is a schematic illustration of a DC-to-AC MMC 1 in direct double-star configuration between an AC network L, which is a three-phase network
5 having currents i_{L1} , i_{L2} and i_{L3} , and a DC network R having the current i_{DC} and the voltage u_{DC} . The AC network may e.g. be a national power distribution network which may have a nominal fundamental frequency (also called power line/mains/utility frequency) of for instance 50 or 60 Hz. The DC network R may e.g. be for renewable energy production such as including
10 photovoltaic and/or wind power generator(s), or for BESS, HVDC, electric drives etc.

The MMC 1 comprises a plurality of phase legs 11, here three (one per phase of the AC network L), where each phase leg comprises a first (upper) branch (arm) 12a and a second (lower) branch 12b. Each branch 12 comprises a
15 plurality of series connected converter cells 13, and typically also a reactor (shown in black). In the figure, the currents and voltages relating to the first branches 12a are indexed "a" while the currents and voltages relating to the second branches 12b are indexed "b". Typically, each branch 12 comprises the same number of cells 13. Embodiments of the present invention may be
20 particularly useful for a relatively small number of cells per branch, why the number of series connected cells in each branch may be at most 20 cells, e.g. within the range of 5 to 20 cells, or at most 10 cells.

The MMC 1 also comprises a controller 14 which is schematically shown in figure 1. The controller may be a control system comprising a central unit
25 and/or distributed units associated with respective legs 11 or branches 12. The controller 14 may be configured, e.g. by means of computer software, to perform embodiments of the method of the present disclosure.

The MMC 1 may be a medium voltage converter, e.g. having a voltage rating of less than 30 kV (thus being configured for an operating voltage of less than
30 30 kV) and/or a power rating within the range of 10 to 60 MW, e.g. 15 to 30

MW (thus being configured for an operating power within the range of 10 to 60 MW, e.g. 15 to 30 MW).

The converter cells 13 may be any type of conventional MMC cell, such as a type of unipolar (half-bridge) or bipolar (full-bridge, H-bridge) cell. The invention does not require the cells to be bipolar, why at least one, some or all of the cells 13 of each branch 12 may in some embodiments of the invention be unipolar cells. Different types of unipolar and bipolar cells are well-known in the art.

Figure 2 illustrates an example of a bipolar cell 13. The cell comprises an energy storing device 5, here in the form of a capacitor. The capacitor 5 may give rise to voltage ripples, which may be compensated for by means of embodiments of the present invention. The energy storing device 5 may comprise a capacitor arrangement with any number of capacitors in series and/or parallel connection with each other. The cell 13 also comprises four semiconductor switches S, forming the full-bridge (H-bridge) topology in the cell. Similarly, a corresponding unipolar cell 13 comprises only two semiconductor switches S, forming a half-bridge topology. Any number of semiconductor switches may be used, and the cell with four switches shown in the figure is only an example. The semiconductor switches of the bipolar cell are conventionally named in the figure as S1 switch, S2 switch, S3 switch and S4 switch. When the switches S1 and S4 are closed and S2 and S3 are open, the cell is in a +1 state in which a positive voltage will be applied. By opening S1 and S4 switches and closing S2 and S3 switches, this voltage is reversed whereby the cell is in a -1 state and a negative voltage will be applied. Regardless of whether a bipolar or unipolar cell is used, each of the S switches may comprise e.g. an insulated-gate bipolar transistor (IGBT) or a gate commutated thyristor GCT (in which case a snubber circuit may also be needed), for instance an integrated gate commutated thyristor (IGCT), a reverse-conducting IGCT (RC-IGCT) or a bi-mode GCT (BGCT), possibly in combination with an antiparallel one-direction conducting/blocking component such as a diode. In the example of figure 2, each S switch comprises an IGCT and antiparallel diode.

Embodiments of the present invention may be especially advantageous for cells 13 having a relatively low switching frequency, e.g. of at most 125 Hz, e.g. at most 100 Hz or 50 Hz. In some embodiments, the cells of the MMC has a switching frequency equal to the nominal fundamental frequency of the
5 three-phase AC network L, e.g. 50 Hz or 60 Hz.

Medium voltage DC/AC MMCs are expected to be found in e.g. solar or other DC grids, battery energy storage systems and variable speed drives. The latter includes pumped hydro storage plants. In the lower power range, only a few cells are needed. This leads to a low number of voltage levels at the converter
10 phase terminals, which may result in an inferior harmonic performance of the converter 1.

In addition, it is of interest to keep the switching frequency low in order to reduce switching losses and therefore increase the converter's efficiency.

The two aforementioned issues pose significant challenges regarding the
15 product competitiveness, especially in the low power range. Moreover, and even if it might not be desirable, a filter on the three-phase side might be eventually needed in order to meet the AC grid-side harmonic requirements. In this case, a modulation method which facilitates the design of such a filter may be chosen.

20 Conventional methods, such as Carrier-Based Pulse Width Modulation (CB-PWM) are not an option for such operating conditions. Even more advanced modulators based on converter virtual flux and hysteresis (tolerance) bands may not provide in such conditions the required harmonic performance.

The aforementioned shortcomings of the state-of-the-art control and
25 modulation methods may then necessitate the use of OPPs. However, OPPs may not be easily combined with a closed-loop control system for several reasons. First, the discontinuity of the switching angles when varying the modulation index prevents the use of linear controllers due to stability issues. Second, unlike modulation methods with a fixed modulation cycle such as
30 carrier-based pulse width modulation (CB-PWM) and space vector

modulation (SVM), OPPs are associated with a non-zero ripple current at regularly-spaced sampling instants. The bandwidth of a conventional current controller thus has to be slow, limiting the capability of the controller to reject disturbances and to react to the transients.

- 5 Further, OPPs are typically calculated considering ideal conditions, i.e., neglecting system disturbances. This limits the applicability of OPPs to MMC configurations without additional control actions, due to the considerable inherent capacitor voltage ripples and other system non-idealities.

In accordance with the present disclosure, the above-mentioned problems
 10 are tackled by means of a closed-loop pulse pattern control concept. The closed-loop pulse pattern control concept is illustrated in figure 3 in which functionality of an embodiment of the controller 14 is schematically shown. An MP3C control 32 (which typically is a non-linear control) is used to adjust the OPP 31 which has been calculated (in the controller 14 or externally of the
 15 controller and then received by said controller 14) for ideal conditions. Given the active and reactive power references P_g^* and Q_g^* , respectively, the estimate of the virtual grid flux vector and the grid inductance, the ideal reference of the fundamental virtual converter flux vector is determined.

The magnitude of the fundamental virtual converter flux vector reference is
 20 translated into a desired modulation index m^* and the respective argument to a rotating angle reference θ^* . If the desired modulation index differs by a certain threshold from the actual modulation index a (new) switching sequence is loaded with the desired pulse number d . The integral of the switched voltage waveform constitutes the reference trajectory of the
 25 instantaneous virtual converter flux vector $\psi_{c,\alpha\beta}^*$.

The controller forces the virtual converter flux $\psi_{c,\alpha\beta}$ to track the OPP flux trajectory. To achieve this, the controller aims to minimize the flux error in stationary reference frame,

$$\psi_{e,\alpha\beta} = \psi_{c,\alpha\beta}^* - \psi_{c,\alpha\beta} \quad (1)$$

by modifying the switching angles of the OPP. In the simplest case, a dead-beat (DB) controller can be used in the abc -coordinates, leading to the correction times

$$\Delta t = \frac{\psi_e}{-duV_{lvi}} \quad (2)$$

5 where ψ_e denotes the flux error in abc -coordinates, $du = U_i - U_{i-1}$ denotes the change in the switch position of the switching sequence and V_{lvi} corresponds to the voltage step in the phase voltage waveform. Thus, the MP3C may have a ‘deadbeat’ nature, but not in the sense of trying to bring the error to zero at the next sampling time instant. Instead the error may be
 10 put to zero within the next switching transitions that follow in at least two system phases. At least two phases may be needed to bring the error to zero in a three-phase system, which is controlled using an $\alpha\beta$ coordinate transformation.

This pulse pattern control method is referred to as Model Predictive Pulse
 15 Pattern Control (MP3C). The flux error is minimized over a prediction horizon by computing a modified switching sequence. Only the first part of the switching sequence within the time interval $t, t + T_s$ is applied to the converter, where T_s denotes the sampling interval. At the next sampling instant, using new measurements (or estimates), the flux error minimization
 20 is repeated over a shifted or receding prediction horizon. This so-called receding horizon policy provides feedback and ensures that the controller is robust to parameter uncertainties. The condition on the horizon is to have at least two switching events in two different phases in order to be able to drive the flux error to zero in the $\alpha\beta$ -reference frame.

25 A few constraints may also be added to the control problem:

- A switching transition cannot be moved to the past (or the previous sampling interval).
- A switching transition cannot be moved before or after another switching transition in that phase.

It is noted that such a three-phase control and modulation approach is beneficial for switching frequency reduction, as any of the three phases can be used for flux error minimization. This is contrary to a modulation concept that is based on a single branch. Furthermore, thanks to the dead-beat
5 control behaviour of the pattern controller, fast current and power responses may be achieved during transients. The term 'fast' herein implies that the MP3C may not act on the average (fundamental) waveform, like a conventional 'slow' controller would do. Instead, it may act rather on the instantaneous quantity, which is the OPP switching control signal (by shifting
10 the switching times). This gives a faster response time, e.g. instead of milliseconds, the control could act on the system in the range of microseconds.

Another MP3C variety formulates a quadratic program (QP). The QP may be solved using for example an active set method. MP3C is in itself known, but
15 for other converter topologies, see e.g. US 8,766,570 and the Institute of Electrical and Electronics Engineers (IEEE) paper "Model predictive pulse pattern control" to T. Geyer, N. Oikonomou, G. Papafotiou and F.D. Kieferndorf, IEEE Trans. on Industry Applications, vol. 48, no. 2, pp. 663-676, Mar./Apr. 2012.

20 Two different types of modulations can be applied to the double star-configured DC/AC MMC 1. They are tightly linked to the number of levels in the phase voltage waveform and influence the way the circulating current control can be performed. They are graphically presented in figures 4a and 4b, respectively, where the voltage of the phase-leg 11 is given by the
25 combination of the respective voltages of the first branch 12a and the second branch 12b, since there is in this example no circulating current to consider. Figure 4a illustrates an embodiment of $N+1$ modulation, where the first and second branch modulations are symmetrical in the absence of a circulating current. Figure 4b illustrates an embodiment of $2N+1$ modulation, where if
30 the dotted lines are followed, the $N-1$ redundant level is obtained, else the $N+1$ redundant level is obtained.

$N+1$ modulation: both the first and second branches 12 of the same phase-leg 11 are switched synchronously in opposite manner when a switching event occurs on the phase voltage pattern. The sum of the inserted cells in the first branch 12a (n_1) and in the second branch 12b (n_2) per phase-leg 11 is always
 5 equal to N : $n_1 + n_2 = N$.

$2N+1$ modulation: only one of the two branches 12 is switched when a switching event occurs on the phase voltage pattern. As a result, the number of voltage levels is almost doubled for the same switching frequency. The first and second branches are switched in an asynchronous manner, and as a
 10 consequence the sum of inserted cells 13 per phase-leg 11 is not anymore always equal to N , but can take three values: $n_1 + n_2 = \{N-1, N, N+1\}$.

If a circulating current is used for balancing the power of different branches 12, the circulating current control may be performed through the timing/insertion of the so-called redundant levels. The redundant levels are
 15 any sum of positive and negative branch insertion indices that do not equal N . The closest neighbours are $N+1$ and $N-1$, and they may be accessed without increasing the cell switching frequency.

In $N+1$ modulation, those redundant levels have to be actively inserted by switching transition advance/delay in a symmetrical manner between the
 20 first and second branches 12. A symmetrical correction reduces the negative impact on the three-phase converter flux.

In $2N+1$ modulation, the redundant levels are present by default and the only degree of freedom is their selection (either $N+1$ or $N-1$), but not their duration. This affects the way the circulating current can be controlled, as
 25 well as the possible achievable control performances.

$N+1$ modulation type: The circulating current control for $N+1$ modulation is added to the existing grid flux MP3C control 32. The circulating current error is translated into a correction time that will be applied in an opposite manner (different sign) to the first and second branches 12 of the same phase-leg 11,

minimizing the impact on the grid flux. The correction time may be calculated as:

$$dt_{corr} = -2L_{br} \frac{\Delta i_{circ}}{v_{lvl}} \quad (3)$$

It has the particularity to be intermittent, i.e., the circulating current control is effective only in the vicinity of the switching transitions. For the control of the circulating current, a so called Dead-Beat (DB) Circulating Current Control, DBC3, may be used.

It is also noted that some special cases might arise and may be handled:

- 10 - A switching transition originally occurring in $[t, t + T_s]$ might be shifted to the next sampling interval in one of the two branches 12. A memory element may therefore be added, which may momentarily store the transition until it should be applied. If the switching transition is lost, the phase pattern might contain some undesirable discontinuities.
- 15 - A switching transition originally occurring in $[t + T_s, t + 2T_s]$ might be shifted to the current sampling interval in one of the two branches. A memory element may therefore be added, which may momentarily store the transition until it is applied in the other branch. In addition, the pattern pointer has to be incremented: the original switching transition in the phase cannot be modified anymore to control the converter phase flux.
- 20

$2N+1$ modulation: The $2N+1$ modulation may not be deployed without a switching event distribution logic. This logic selects between the $N+1$ and $N-1$ redundant levels ($N-x / N+x$ redundant levels or additional $N-1 / N+1$ redundant levels are also possible through a pulse insertion technique at the expense of increased switching frequency) in a hysteresis control manner. This implies that it is reacting on the sign of the circulating current error $i_{circ,err} = i_{circ}^* - i_{circ}$. With a low number of cells 13 in a branch 12, the

circulating current may feature a strong ripple at a low frequency (but higher than the switching frequency). The peak-to-peak circulating current ripple may be directly estimated from the generated OPP:

$$\Delta i_{circ,max} = \frac{V_{|V|}^*/2\Delta t_{red,max}}{2L_{br}} \quad (4)$$

5 where $\Delta t_{red,max}$ is the maximum duration of a redundant level in the pattern. Note that this value changes for each modulation index m . It may be important to emphasize that this high ripple is not visible in the three-phase grid currents. For possible transitions with $2N+1$ modulation, the switching transition information may be combined with the current switch position in
10 order to define a Level Selector (LS) table (either $N+1$ or $N-1$ redundant level).

Only one exception case is considered here: between two consecutive sampling intervals $[t, t + T_s]$ and $[t + T_s, t + 2T_s]$, it might occur that the sign of the circulating current error changes. It is even more likely to happen as
15 the circulating current ripple is high. This would mean that the applied redundant level should be modified ($N+1 \leftrightarrow N-1$). However, this may not be possible without increasing the switching frequency. As a consequence, the applied redundant level is locked until a non-redundant level is applied.

The circulating current may be regulated along a reference trajectory with a
20 certain amplitude and frequency.

The proposed closed loop-controlled OPPs and fast circulating current controllers may be interfaced in a straightforward manner to the higher level MMC inner voltage control. This is illustrated in figure 5a for the cases of $N+1$ level modulation and in figure 5b for the $2N+1$ level modulation.

25 With $N+1$ level modulation, a circulating current controller 53 in the form of a DBC3 53a is used with input from the MMC voltage control 51 as illustrated in figure 5a.

With $2N+1$ level modulation, a circulating current controller 53 in the form of a hysteresis circulating current control (\square) in combination with a Level Selector 53b is used with input from the MMC voltage control 51 as illustrated in figure 5b.

- 5 The MMC voltage control 51 (upper layer MMC inner voltage control) is responsible for controlling the average converter DC-link voltage (total energy) by means of adjusting the three-phase power reference as needed. It also ensures that no unbalance occurs between the sums of the cell capacitors 5 voltages in each branch 12. This is achieved by introducing appropriate
- 10 circulating currents i_{circ}^* with specific amplitudes and frequencies. It is noted that other feed-forward terms may be also added to the circulating current references $i_{circ,ff}^*$ for achieving different purposes, such as capacitor voltage ripple minimization etc. A conventional sorting/selection algorithm 52 may be used to choose the cells 13 to switch.
- 15 As previously mentioned, an argument for using OPPs 31 is the ability of actively shaping the spectrum through an optimization procedure. The whole converter control system has been simulated.

For the cases of $N+1$ as well as $2N+1$ modulation, the converter 1 is operated at a switching frequency of $f_{sw} = 50$ Hz. In both cases, the voltage total

20 demand distortion (TDD) was minimized. It is clear that the TDD in the $2N+1$ case is lower, since there are twice as many degrees of freedoms for minimizing it. However, this case has a higher impact on the inner converter magnitudes, e.g., a larger branch reactor is needed in order to minimize the higher branch current ripple.

- 25 Especially for the $N+1$ case, the results showed a very discrete spectrum without the presence of either even harmonics or interharmonics. In the specific example, no restriction was put on specific harmonics, therefore lower order ones, such as the 7th and 11th do appear, for which the relevant grid standards normally allow for a higher amplitude.

Moreover, it might be beneficial to cancel such low order harmonics, especially in the presence of AC grid side resonances that tend to threaten the fulfilment of such limits. According to the degree of freedom, i.e., the pulse number d , several harmonics may be limited or even cancelled. For an $N+1$ modulation the voltage TDD was minimized while imposing constraints on the 7th and 11th harmonics using specific weighting factors. The harmonic energy content may be either placed in triplen harmonics, which are cancelled out on a line voltage level and/or shifted to higher frequencies, facilitating the design of a grid filter.

Thanks to its receding horizon policy and despite the low apparent branch switching frequency, the MP3C strategy offers good performance regarding power transients. When the power reference changes, the modulation index is updated according to the new power reference. A three-phase power step may be tracked within a few milliseconds. Moreover, the circulating current control makes it possible to track any changes in the reference in a rapid manner. Undesired overshoots in the circulating current reference may be avoided by properly tuning the total MMC energy controller or by controlling the DC part of the circulating current directly on a DC-link level.

The transient performance may be even further increased with the pulse insertion method. If, alternatively, a slower transient response is desired, the reference may be changed in a ramped rather than a stepped manner.

The capacitor voltages, for reasons of grid overvoltage handling or redundancy reasons, may not be expected to sum up to u_{DC} per phase-leg. This implies that the number of cells inserted in the first and second branches no longer meet the equations

$$\begin{cases} n_{up} = \frac{N}{2} - u_L \\ n_{low} = \frac{N}{2} + u_L \end{cases} \quad (5)$$

as in the ideal case. This implies the adaptation of the integer part $N/2$ to one of the smaller integers, e.g. $N/2-1$. For instance, three cells may have to be

permanently inserted for each of the first and second branches 12 and would replace the $N/2$ terms in equation (5). The remaining part, i.e., $V_{circ,DC} = V_{bus}^* - 2n_{DC}V_c^*$ is inherently provided by the total phase-leg capacitor voltage controllers. That component may however remain small in order not to

5 compromise the circulating current control due to a reduction of v_{circ} , since a fraction of it may be used to accommodate the DC voltage. Consequently, it may be convenient to coordinate V_c^* with V_{bus}^* to always operate close to an even integer multiple of V_c^* ($V_{bus}^* \approx 2n_{DC}V_c^*$).

The OPP calculator or loader 31 may typically consider an odd number of

10 voltage levels. With an even number of voltage levels, the switching transitions at 0 and π are fixed, leading to the same number of degrees of freedom $d-1$ as an even number of cells corresponding to $(N-1)$. The definition of the inserted branch cell number should avoid running into non-integer values.

15 The DC current of the DC network R may be explicitly controlled by adjusting V_{bus}^* . In this way, the total converter energy may be controlled through the DC terminal rather than through the AC terminal. Note that the feed-forward term $I_{DC,ff}$ is optional. The term n_{DC} replaces $N/2$ in equation (5).

Figure 6 is a schematic flow chart of an embodiment of the method of the

20 present invention. The method may be performed in/by a controller 14 of the MMC 1. The method is for controlling a direct DC-to-AC MMC 1 having a three-phase AC side connected to a three-phase AC network L and having a DC side connected to a DC network R. The MMC has a double-star topology with a plurality of phase-legs 11, each phase-leg having a first branch 12a and

25 a second branch 12b, each of the first and second branches 12 comprising a plurality of series connected converter cells 13. An OPP 31 for the MMC is obtained M1, e.g. calculated offline internally in the controller 14 or externally of the controller and then received by said controller. Then, the OPP is adapted M2 to the MMC 1 by means of closed-loop pulse pattern

30 control 32, e.g. MP3C. Based on the adapted M2 OPP 31, firing signals (for

switching the semiconductor switches S) are sent M₃ to the plurality of cells 13 of each branch 12 to implement the control of the MMC.

5 The present disclosure has mainly been described above with reference to a few embodiments. However, as is readily appreciated by a person skilled in the art, other embodiments than the ones disclosed above are equally possible within the scope of the present disclosure, as defined by the appended claims.

CLAIMS

1. A method of controlling a DC-to-AC Modular Multilevel Converter, MMC, (1) having a three-phase AC side connected to a three-phase AC network (L) and having a DC side connected to a DC network (R), wherein
5 the MMC has a double-star topology with a plurality of phase-legs (11), each phase-leg having a first branch (12a) and a second branch (12b), each of the first and second branches (12) comprising a plurality of series-connected converter cells (13), the method comprising:

obtaining (M1) an Optimized Pulse Pattern, OPP, (31) for the MMC;

10 adapting (M2) the OPP to the MMC by means of closed-loop pulse pattern control (32), and

based on the adapted (M2) OPP, sending (M3) firing signals to the plurality of cells (13) of each branch (12).
2. The method of claim 1, wherein the closed-loop pulse pattern control
15 (32) has a receding horizon policy.
3. The method of claim 1 or 2, wherein the closed-loop pulse pattern controller (32) is a Model Predictive Pulse Pattern Control, MP3C.
4. The method of any preceding claim, wherein the adaptation (M2) of the OPP comprises circulating current control (53).
- 20 5. The method of claim 4, wherein the circulating current control (53) comprises Dead-Beat Circulating Current Control, DBC3, (53a).
6. The method of claim 4, wherein the circulating current control (53) comprises hysteresis circulating current control (53b).
7. The method of any preceding claim, wherein the obtaining (M1) of an
25 OPP comprises calculating the OPP offline.

8. The method of any preceding claim, wherein the plurality of cells (13) in each branch (12) is at most 20 cells, e.g. within the range of 5 to 20 cells, or at most 10 cells.
9. The method of any preceding claim, wherein the MMC (1) has a
5 switching frequency of less than 125 Hz.
10. The method of any preceding claim, wherein the MMC has a switching frequency equal to a nominal fundamental frequency of the three-phase AC network (L).
11. The method of any preceding claim, wherein the three-phase AC
10 network (L) has a nominal fundamental frequency of 50 or 60 Hz.
12. The method of any preceding claim, wherein the MMC (1) has an operating voltage of less than 30 kV.
13. The method of any preceding claim, wherein at least some, or all, of the plurality of converter cells (13) in each branch (12) are unipolar cells.
- 15 14. A computer program product comprising computer-executable components for causing a controller (14) to perform the method of any preceding claim when the computer-executable components are run on processing circuitry comprised in the controller.
- 20 15. A controller (14) configured for controlling a power converter, the controller comprising:
processing circuitry; and
storage storing instructions executable by said processing circuitry whereby said controller is operative to:
obtain an Optimized Pulse Pattern, OPP, (31) for a DC-to-AC Modular
25 Multilevel Converter, MMC, (1) having a three-phase AC side connected to a three-phase AC network (L) and having a DC side connected to a DC network (R), wherein the MMC has a double-star topology with a plurality of phase-

legs (11), each phase-leg having a first branch (12a) and a second branch (12b), each of the first and second branches (12) comprising a plurality of series connected converter cells (13);

adapt the OPP to the MMC by means of closed-loop pulse pattern control
5 (32), and

based on the adapted OPP, send firing signals to the plurality of cells (13) of each branch (12).

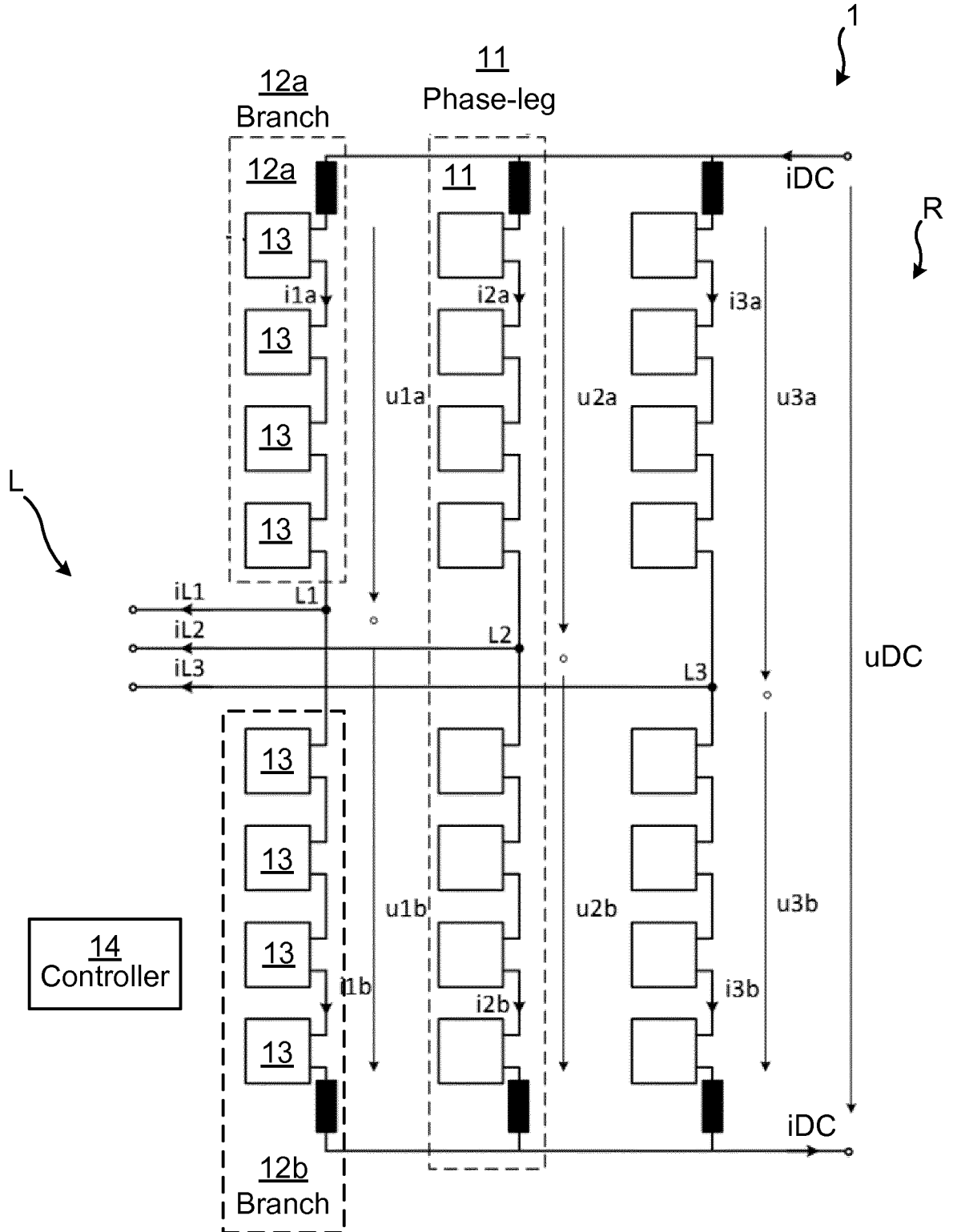


Fig. 1

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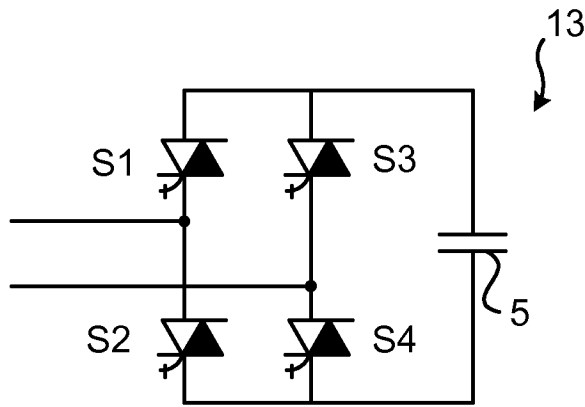


Fig. 2

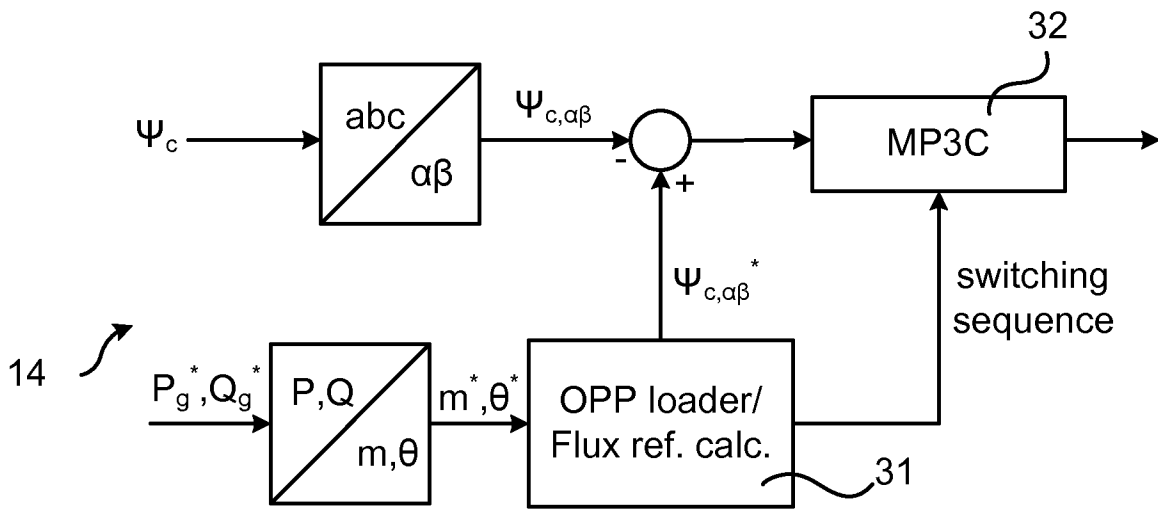


Fig. 3

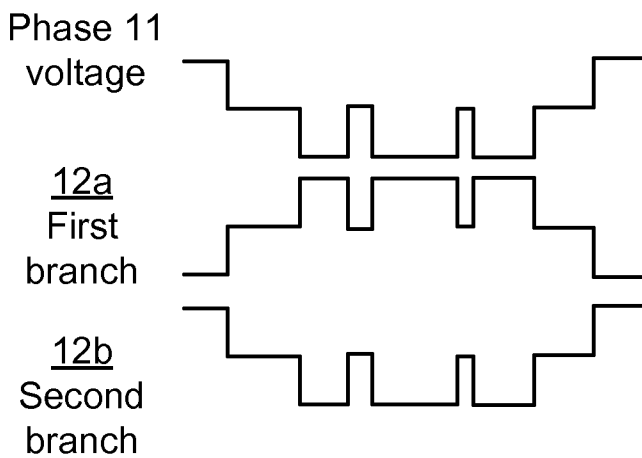


Fig. 4a

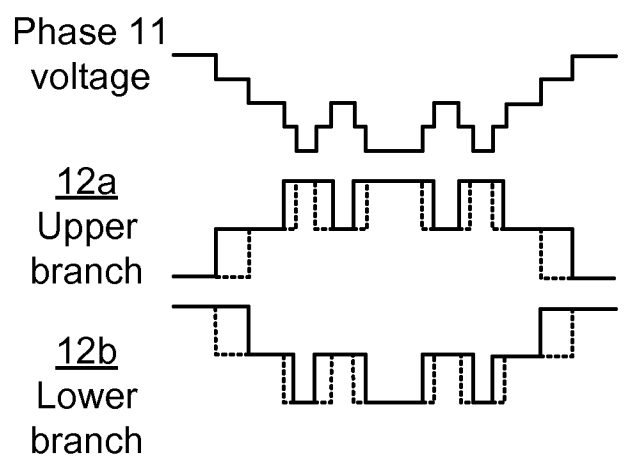


Fig. 4b

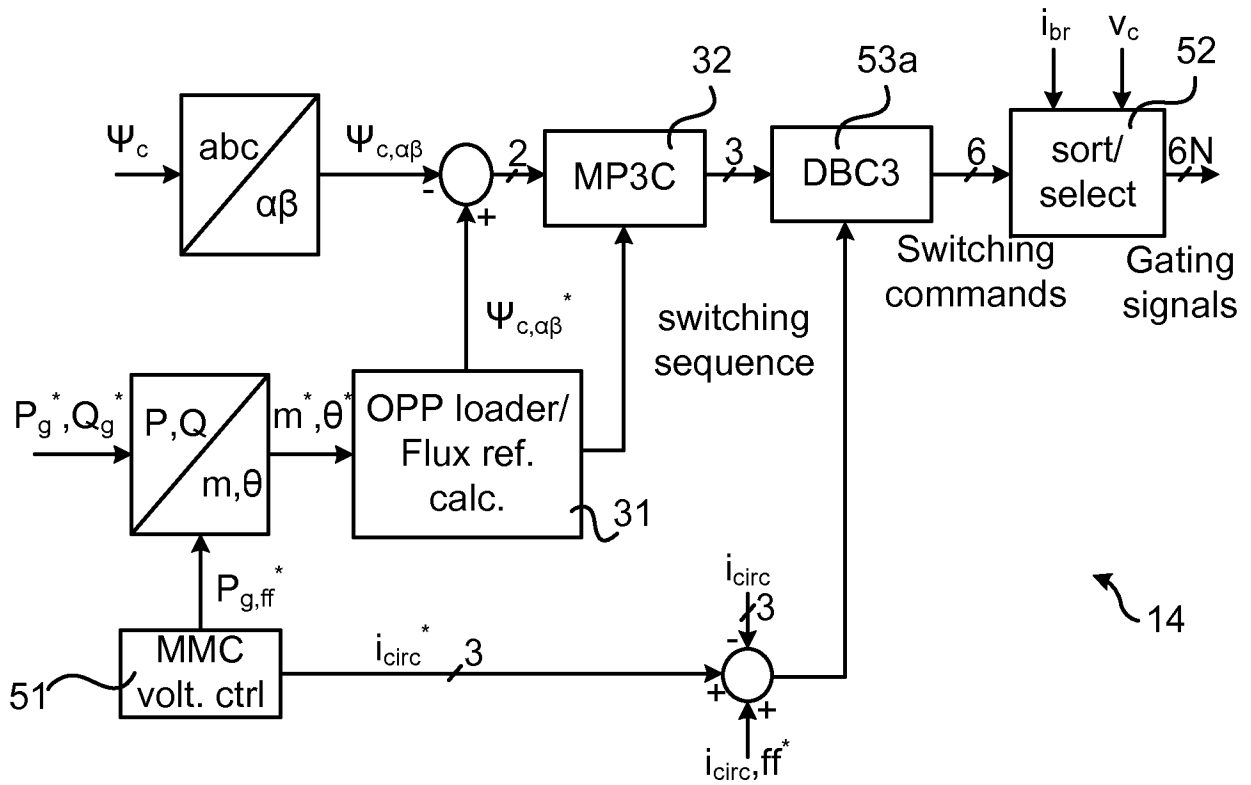


Fig. 5a

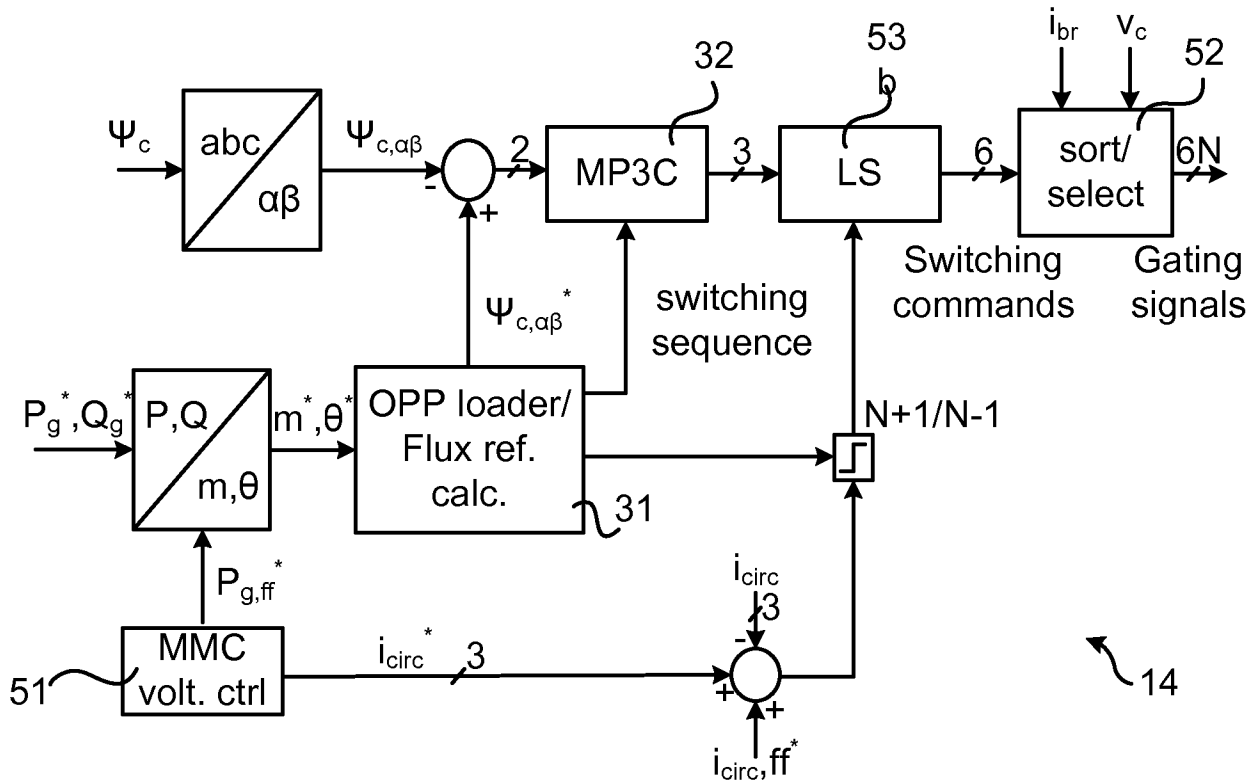


Fig. 5b

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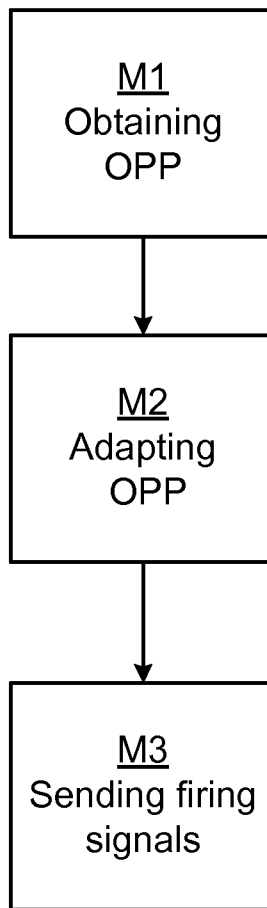


Fig. 6

INTERNATIONAL SEARCH REPORT

International application No
PCT/EP2016/075342

A. CLASSIFICATION OF SUBJECT MATTER
INV. H02M7/483 H02M1/12 H02J3/18
ADD.
According to International Patent Classification (IPC) or to both national classification and IPC

B. FIELDS SEARCHED
Minimum documentation searched (classification system followed by classification symbols)
H02M H02J
Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched

Electronic data base consulted during the international search (name of data base and, where practicable, search terms used)
EPO-Internal, WPI Data

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
X	EP 2 725 706 A1 (ABB TECHNOLOGY AG [CH]) 30 April 2014 (2014-04-30)	1,9-15
Y	paragraph [0004] - paragraph [0005] paragraph [0012] paragraph [0039] paragraph [0036] paragraph [0044] paragraph [0047] paragraph [0055] paragraph [0058] paragraph [0102] - paragraph [0109] figure 1 ----- -/--	2-8

Further documents are listed in the continuation of Box C.

See patent family annex.

* Special categories of cited documents :

<p>"A" document defining the general state of the art which is not considered to be of particular relevance</p> <p>"E" earlier application or patent but published on or after the international filing date</p> <p>"L" document which may throw doubts on priority claim(s) or which is cited to establish the publication date of another citation or other special reason (as specified)</p> <p>"O" document referring to an oral disclosure, use, exhibition or other means</p> <p>"P" document published prior to the international filing date but later than the priority date claimed</p>	<p>"T" later document published after the international filing date or priority date and not in conflict with the application but cited to understand the principle or theory underlying the invention</p> <p>"X" document of particular relevance; the claimed invention cannot be considered novel or cannot be considered to involve an inventive step when the document is taken alone</p> <p>"Y" document of particular relevance; the claimed invention cannot be considered to involve an inventive step when the document is combined with one or more other such documents, such combination being obvious to a person skilled in the art</p> <p>"&" document member of the same patent family</p>
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Date of the actual completion of the international search 14 July 2017	Date of mailing of the international search report 25/07/2017
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Name and mailing address of the ISA/ European Patent Office, P.B. 5818 Patentlaan 2 NL - 2280 HV Rijswijk Tel. (+31-70) 340-2040, Fax: (+31-70) 340-3016	Authorized officer Fribert, Jan
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INTERNATIONAL SEARCH REPORT

International application No
PCT/EP2016/075342

C(Continuation). DOCUMENTS CONSIDERED TO BE RELEVANT		
Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
Y	<p>WO 2015/055444 A1 (ABB TECHNOLOGY AG [CH]) 23 April 2015 (2015-04-23) page 2, line 17 - line 23 page 5, line 30 - line 33 page 14, line 9 - line 32 page 17, line 19 - line 20 figure 1</p> <p style="text-align: center;">-----</p>	1-15
Y	<p>WO 2014/046555 A1 (AUCKLAND UNISERVICES LTD [NZ]; MADAWALA UDAYA KUMARA [NZ]; RIAR BALJIT) 27 March 2014 (2014-03-27) page 10, line 14 - line 25 page 1, line 31 - page 2, line 5 figure 2a</p> <p style="text-align: center;">-----</p>	1-15
Y	<p>TOBIAS GEYER ET AL: "Model Predictive Pulse Pattern Control", IEEE TRANSACTIONS ON INDUSTRY APPLICATIONS, IEEE SERVICE CENTER, PISCATAWAY, NJ, US, vol. 48, no. 2, 1 March 2012 (2012-03-01), pages 663-676, XP011434186, ISSN: 0093-9994, DOI: 10.1109/TIA.2011.2181289 cited in the application abstract page 664; figures 1, 2</p> <p style="text-align: center;">-----</p>	1-15

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Information on patent family members

International application No

PCT/EP2016/075342

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			WO 2014046555 A1 27-03-2014
