





l'intérieur du pneumatique. Le transpondeur comprend un circuit (226) pour la gestion des créneaux de temps ( $W_T$  et  $W_P$ ) pendant lesquels des mesures en temps réel de température et de pression sont effectuées, et pour stocker (236) les données de calibration, l'identifiant du transpondeur et des nombres du même genre, et pour l'émission de cette information dans un flux de données (Figure 3C) destiné au lecteur/interrogateur. Des conditions de température excessive peuvent être aussi captées (MTMS 218) et incluses dans le flux de données. Le circuit du transpondeur est, de préférence, implanté sur un circuit intégré unique (204), à l'aide de technologie CMOS, et avec peu de composants extérieurs au circuit intégré. Le transpondeur est, de préférence, passif, obtenant sa puissance de service grâce à un signal RF fourni par le lecteur/interrogateur externe. Des données ( $N_T$ ) indicatives de température et des données ( $N_P$ ) indicatives de pression sont émises ensemble au lecteur/interrogateur simultanément avec des données de calibration. Les données de calibration stockées par le transpondeur, émises dans le flux de données, sont représentées par une pente de  $N_T/N_P$ , ou par le rapport du relevé de température divisé par le relevé de pression, déterminé pendant la calibration du transpondeur.

includes circuitry (226) for controlling windows of time ( $W_T$  and  $W_P$ ) during which real-time temperature and pressure measurements are made, and for storing (236) calibration data, transponder ID number and the like, and for transmitting this information in a data stream (Figure 3C) to the reader/interrogator. An excessive temperature condition may also be sensed (MTMS 218) and included in the data stream. The circuitry of the transponder is preferably implemented on a single IC chip (204), using CMOS technology, with few components external to the IC chip. The transponder is preferably passive, deriving its operating power from an RF signal provided by the external reader/interrogator. Data ( $N_T$ ) indicative of temperature and data ( $N_P$ ) indicative of pressure are both transmitted to the reader/interrogator, along with calibration data. A calibration data stored by the transponder and transmitted in the data stream is a slope of  $N_T/N_P$ , or the "ratioed" response of the temperature count divided by the pressure count, which is determined during calibration of the transponder.

PCT

WORLD INTELLECTUAL PROPERTY ORGANIZATION  
International Bureau

## INTERNATIONAL APPLICATION PUBLISHED UNDER THE PATENT COOPERATION TREATY (PCT)

(51) International Patent Classification<sup>6</sup> :

G01K 7/01, B60C 23/04

A1

(11) International Publication Number:

WO 99/53279

(43) International Publication Date:

21 October 1999 (21.10.99)

(21) International Application Number: PCT/US98/07575

(22) International Filing Date: 14 April 1998 (14.04.98)

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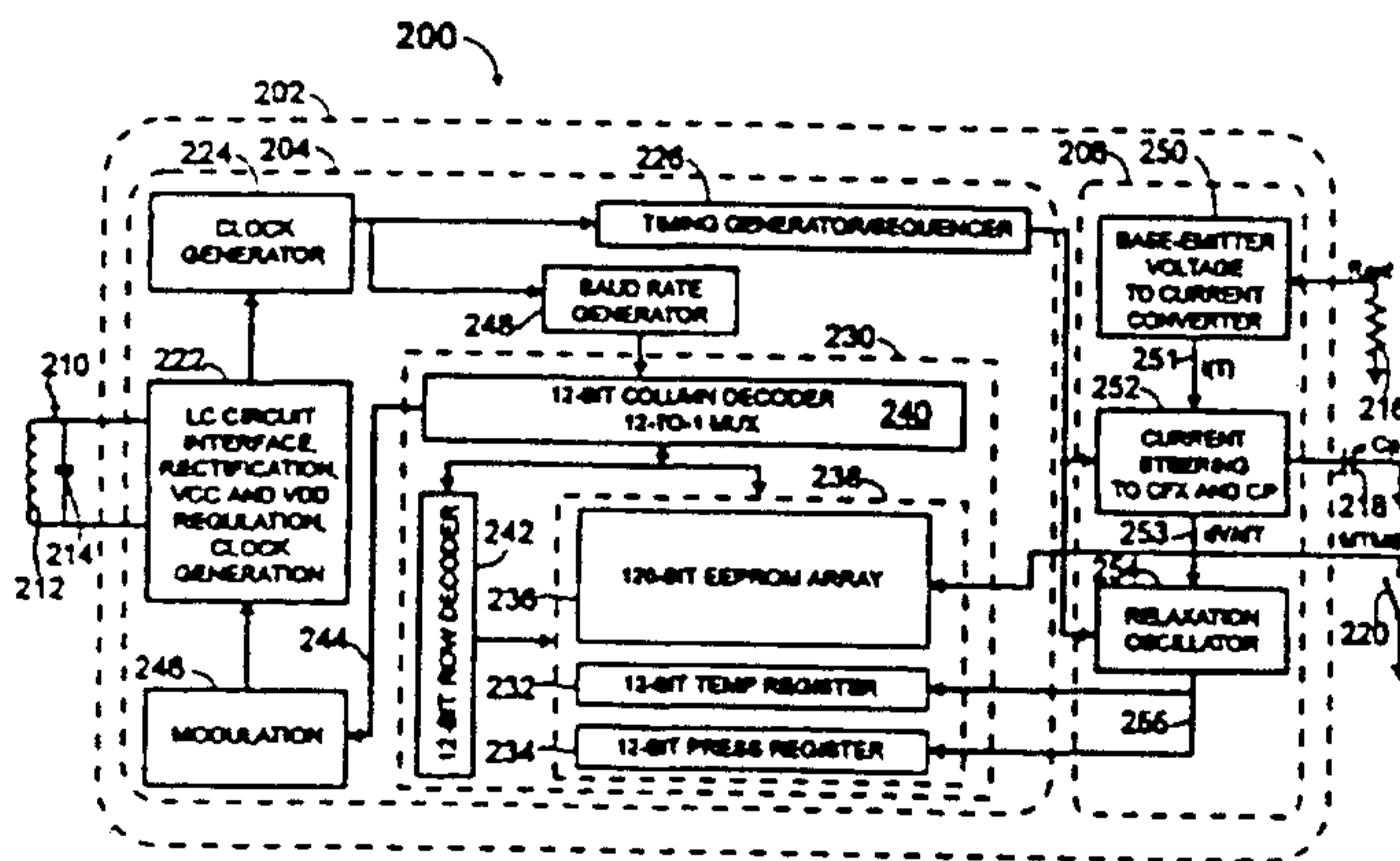
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BY, CA, CH, CN, CU, CZ, DE, DK, EE, ES, FI, GB, GE,  
GH, GM, GW, HU, ID, IL, IS, JP, KE, KG, KP, KR, KZ,  
LC, LK, LR, LS, LT, LU, LV, MD, MG, MK, MN, MW,  
MX, NO, NZ, PL, PT, RO, RU, SD, SE, SG, SI, SK, SL,  
TJ, TM, TR, TT, UA, UG, US, UZ, VN, YU, ZW, ARIPO  
patent (GH, GM, KE, LS, MW, SD, SZ, UG, ZW), Eurasian  
patent (AM, AZ, BY, KG, KZ, MD, RU, TJ, TM), European  
patent (AT, BE, CH, CY, DE, DK, ES, FI, FR, GB, GR,  
IE, IT, LU, MC, NL, PT, SE), OAPI patent (BF, BJ, CF,  
CG, CI, CM, GA, GN, ML, MR, NE, SN, TD, TG).

Published

With international search report.

(54) Title: METHOD AND APPARATUS FOR MEASURING TEMPERATURE WITH AN INTEGRATED CIRCUIT DEVICE



## (57) Abstract

A temperature-sensor is implemented with a temperature-sensitive component (Q1) of an IC chip which functions as a radio frequency (RF) transponder (200) capable of measuring parameters associated with an object and transmitting data to an external reader/interrogator (106, 400). In use with a pneumatic tire (104), the transponder measures temperature and pressure within the tire. The transponder includes circuitry (226) for controlling windows of time ( $W_T$  and  $W_P$ ) during which real-time temperature and pressure measurements are made, and for storing (236) calibration data, transponder ID number and the like, and for transmitting this information in a data stream (Figure 3C) to the reader/interrogator. An excessive temperature condition may also be sensed (MTMS 218) and included in the data stream. The circuitry of the transponder is preferably implemented on a single IC chip (204), using CMOS technology, with few components external to the IC chip. The transponder is preferably passive, deriving its operating power from an RF signal provided by the external reader/interrogator. Data ( $N_T$ ) indicative of temperature and data ( $N_P$ ) indicative of pressure are both transmitted to the reader/interrogator, along with calibration data. A calibration data stored by the transponder and transmitted in the data stream is a slope of  $N_T/N_P$ , or the "ratioed" response of the temperature count divided by the pressure count, which is determined during calibration of the transponder.

METHOD AND APPARATUS FOR MEASURING  
TEMPERATURE WITH AN INTEGRATED CIRCUIT DEVICE

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TECHNICAL FIELD OF THE INVENTION

The present invention relates to the measurement of temperature and, more particularly, to measuring temperature with a device that is incorporated into an integrated circuit (IC) chip having additional (i.e. other than temperature-sensing) functionality.

BACKGROUND OF THE INVENTION

A first type of temperature-sensing device is capable of outputting a state signal indicative of whether a sensed temperature is either above or below a predetermined threshold temperature. A household thermostat is exemplary of such a threshold-sensing device. A second type of temperature-sensing device is capable of sensing temperature across a range of temperatures, and outputting a signal which varies in magnitude in proportion to the measured temperature. An electronic clinical thermometer is exemplary of such a temperature-sensing device.

The present invention is directed to the type of temperature-sensing device which is capable of outputting a signal which varies in magnitude in proportion to a sensed temperature, such a device being referred to hereinafter as a "temperature-measuring" device.

The present invention is further directed to sensing temperature with a temperature-measuring device which is implemented on an integrated circuit (IC) chip, the IC chip having intended functionality other than temperature measurement.

United States Patent No. 5,039,878 (08/77), incorporated in its entirety by reference herein, discloses a temperature sensing circuit. A semiconductor junction device (D1) integrated on an integrated circuit (IC) chip is used to generate a first signal (V1) having a known variation with temperature. A second signal (V2) is generated by passing a current (I2) which is proportional to absolute temperature

through a resistor (R1), and also has a known variation with temperature which is opposite in sign to that of the first signal (V1). The two signals are compared to generate an output signal which is dependent on whether the temperature of the chip is below or above a predetermined threshold temperature. In this implementation of a temperature sensing circuit, the junction device (D1) is explicitly and advertently relieved of the temperature-detecting function (see column 1, lines 55-56).

The aforementioned United States Patent No. 5,039,878 is representative of a temperature-sensing application wherein it is desired to sense the temperature of an operating IC chip, it being generally well-known that heat generated (dissipated) by the operation of electronic components is a source of concern and difficulty in many electronic systems, especially in those operating in enclosed, unventilated spaces, as well as those in high-performance miniaturized systems. The mechanisms of heat-generation in electronic systems are well known and understood. In essence, any process (e.g., an operating electronic system) which consumes power generates heat. In the case of an electronic circuit, the components of the circuit heat up, which, in turn, heats up anything in contact with them, including the surrounding air.

Other prior art applications for temperature-sensing devices include: controlling or stabilizing the operating temperature of circuit elements, the precision of which is affected either by ambient temperature changes or temperature changes caused by current flow in the circuit element itself; and controlling a supply of energy to other (than the temperature-sensing) circuit elements to prevent their breakdown due to excessive temperature rise (e.g., overheating).

Reference is made to the following U.S. Patents, each of which is incorporated in its entirety herein: 3,703,651; 4,044,371; 4,854,731; 4,952,865; 4,970,497; 5,063,307;

5,213,416; 5,396,120; 5,639,163; and 5,686,858.

As mentioned hereinabove, the present invention is directed to method and apparatus for measuring temperature over a range of temperatures. Although preferably implemented on-chip, the purpose is not to regulate the operation of the IC chip itself, but rather to monitor an ambient temperature in the vicinity of the IC chip, such as the temperature within a pneumatic tire. In the main hereinafter, method and apparatus for sensing ambient temperature with a transponder associated with the pneumatic tire is discussed.

Transponder or transceiver type identification systems are well known, and generally are capable of receiving an incoming interrogation signal and responding thereto by generating and transmitting an outgoing responsive signal. The outgoing responsive signal, in turn, is modulated or otherwise encoded so as to uniquely identify or label the particular object to which the transponder element is affixed. An example of such a transponder type identification system is disclosed in U.S. Patent No. 4,857,893, issued 15 August 1989 to Carroll and incorporated in its entirety herein. This patent describes a transponder device which receives a carrier signal from an interrogator unit. This carrier signal, of frequency  $F$ , is rectified by a rectifying circuit in order to generate operating power. Alternatively, the addition of a hybrid battery allows device to be converted into a self-powered beacon device. Logic/timing circuits derive a clock signal and second carrier signal of frequency  $F/n$  from the received carrier signal. A uniquely-identifying data word is stored in a Programmable Read-Only Memory (PROM). The data word is encoded and mixed with the carrier signal in a balanced modulator circuit, the output of which is transmitted to the interrogator unit where it is decoded and used as an identifying signal. All electrical circuits of the transponder device are realized on the same monolithic semiconductor chip which may be implemented as a

Complementary Metal Oxide Semiconductor (CMOS) device.

In the manufacture of pneumatic tires, it is desirable to uniquely identify each tire as soon as possible during the course of its fabrication. This is generally done by  
5 assigning an identification (ID) number to each tire. The ability to uniquely identify tires throughout their manufacture is particularly valuable in quality control in order that the source of manufacturing problems can readily be ascertained. For example, statistical process control and  
10 other methods can be used with tire identification to detect process parameters that are going out of specification to detect machinery wear, failure, or maladjustment. The identification information should be easily discernible throughout the manufacturing process, including throughout  
15 post-manufacturing (e.g., inventory control) stages.

It is also beneficial to be able to uniquely identify a tire throughout its service life (use), for example for warranty determination, and retreading of the tire should not adversely affect the ability to identify the tire. It is  
20 also important that the tire identification be readily discernible when the tire is mounted on a steel or aluminum rim (as is normally the case), including when the rim is one of a pair of rims in a dual wheel assembly (as is common with tractor trailers).

Aside from being able to uniquely identify a tire at various stages in its manufacture and service life, it is beneficial to be able to monitor tire pressure when the tire is in use. As is known, proper tire inflation is important to proper tire performance, including road-handling, wear,  
25 and the like.  
30

U.S. Patent No. 4,578,992 issued 01 April 1986 to Galasko, et al. and incorporated in its entirety herein, discloses a tire pressure indicating device including a coil and a pressure-sensitive capacitor forming a passive  
35 oscillatory circuit having a natural resonant frequency which varies with tire pressure due to changes caused to the capacitance value of the capacitor. The circuit is energized

by pulses supplied by a coil positioned outside the tire and secured to the vehicle, and the natural frequency of the passive oscillatory circuit is detected. The natural frequency of the coil/capacitor circuit is indicative of the pressure on the pressure-sensitive capacitor.

The use of radio frequency (RF) transponders, located either within the tire or on a rim for the tire, in conjunction with electronic circuitry for transmitting a RF signal carrying tire inflation (pressure) data, is also well known.

An example of a RF transponder suitable to be installed in the carcass of a pneumatic vehicle tire is disclosed in U.S. Patent No. 5,451,959 issued 19 September 1995 to Schuermann and incorporated in its entirety herein. This patent describes a transponder system comprising an interrogation unit for communicating with a plurality of responder units. The responder unit contains a parallel resonant circuit having a coil and a capacitor for reception of a RF interrogation pulse. Connected to the parallel resonant circuit is a capacitor serving as an energy accumulator. A processor may be provided for receiving input signals from a sensor which responds to physical parameters in the environment of the responder unit, for example to the ambient temperature, the ambient pressure or the like. The sensor could for example be an air-pressure sensitive sensor. In this case the responder unit can be installed in the carcass of a vehicle pneumatic tire and, with the aid of an interrogation unit contained in the vehicle, it is possible to continuously monitor the air pressure in the tire.

Another example of a RF transponder suitable to be installed in the a pneumatic vehicle tire is disclosed in U.S. Patent No. 5,581,023 issued 03 December 1996 to Handfield, et al., and incorporated in its entirety herein. This patent describes a transponder and a receiving unit, preferably one transponder for each vehicle tire, and the transponder may be entirely disposed within the vehicle tire.

The transponder includes a pressure sensor, and may include various other sensors such as a temperature sensor. An Application-Specific Integrated Circuit (ASIC) embodiment of the transponder is described. With reference to Figure 9 of the patent, the ASIC (300) includes an oscillator (322) controlled by an external crystal (325), a constant current device (310) providing current flowing through an external variable-resistance pressure sensor (327), a window comparator circuit (324) having a lower threshold for reporting pressure information established by external resistors (329 and 331) connected in a voltage-divider arrangement, and an upper threshold controlled by an external variable resistor (333). A number of three-position jumpers (328) are utilized to program a unique transponder unit serial number during its manufacture. The ASIC (300) is powered by an external battery (318), and a transmitting circuit (312) is external to the ASIC (300).

Another example of a RF transponder suitable to be installed in a pneumatic vehicle tire is disclosed in U.S. Patent No. 5,661,651 issued 26 August 1997 to Geschke, et al. and incorporated in its entirety herein. This patent describes a wireless system for monitoring vehicle parameters, such as tire pressure. RF signals transmitted from different tires may be distinguished based upon the frequency of the transmitted signal. In order to sense the pressure inside a tire, tire pressure monitoring systems utilize a pressure sensor located within the tire. Figure 2 of this patent shows the preferred structure for a parameter sensor and transmitter circuit when used to monitor the pressure inside a vehicle's tire. Parameter sensor and transmitter circuit (20) includes a pressure-to-voltage transducer (21) and a battery-powered power supply circuit (24).

The need to monitor tire pressure when the tire is in use is highlighted in the context of "run-flat" (run deflated) tires, tires which are capable of being used in a completely deflated condition. Such run-flat tires may

incorporate reinforced sidewalls, mechanisms for securing the tire bead to the rim, and a non-pneumatic tire (donut) within the pneumatic tire to enable a driver to maintain control over the vehicle after a catastrophic pressure loss, and are  
5 evolving to the point where it is becoming less and less noticeable to the driver that the tire has become deflated. The broad purpose behind using run-flat tires is to enable a driver of a vehicle to continue driving on a deflated  
10 pneumatic tire for a limited distance (e.g., 50 miles, or 80 kilometers) prior to getting the tire repaired, rather than stopping on the side of the road to repair the deflated tire.

Hence, it is generally desirable to provide a low-pressure warning system within in the vehicle to alert (e.g., via a light on the dashboard, or a buzzer) the driver to the loss  
15 of air in a pneumatic tire. Such warning systems are known, and do not form part of the present invention, per se.

Although the use of pressure transducers in pneumatic tires, in association with electronic circuitry for transmitting pressure data is generally well known, these  
20 pressure-data systems for tires have been plagued by difficulties inherent in the tire environment. Such difficulties include effectively and reliably coupling RF signals into and out of the tire, the rugged use the tire and electronic components are subjected to, as well as the  
25 possibility of deleterious effects on the tire from incorporation of the pressure transducer and electronics in a tire/wheel system. In the context of "passive" RF transponders which are powered by an external reader/interrogator, another problem is generating  
30 predictable and stable voltage levels within the transponder so that the circuitry within the transponder can perform to its design specification.

An example of a pneumatic tire having an integrated circuit (IC) transponder and pressure transducer is disclosed  
35 in commonly-owned U.S. Patent No. 5,218,861, issued 15 June 1993 to Brown, et. al. and incorporated in its entirety by reference herein. This patent describes an RF transponder

mounted within a pneumatic tire. Upon interrogation (polling) by an external RF signal provided by a "reader", the transponder transmits tire identification and tire pressure data in digitally-coded form. The transponder is

5 "passive" in that it is not self-powered, but rather obtains its operating power from the externally-provided RF signal.

The tire has two spaced beads, each including an annular tensile member of wound or cabled steel wire. The transponder antenna is positioned adjacent one of the annular

10 tensile members for electric or magnetic field coupling to the annular tensile member.

Another example of a pneumatic tire having an integrated circuit (IC) transponder and pressure transducer is disclosed in commonly-owned U.S. Patent No. 5,181,975, issued 26

15 January 1993 to Pollack, et. al. and incorporated in its entirety by reference herein. As described in this patent, in a tire that has already been manufactured, the transponder may be attached to an inner surface of the tire by means of a tire patch or other similar material or device.

20 Another example of an RF transponder in a pneumatic tire is disclosed in commonly-owned U.S. Patent No. 4,911,217, issued 27 March 1990 to Dunn, et. al. and incorporated in its entirety by reference herein. This patent describes the transponder having two electrodes, a first of which is

25 positioned such that the average spacing of the first electrode's surface from one of the tire's steel reinforcing components, such as an annular tensile member in its bead or a steel-reinforced ply, is substantially less than the average spacing of the second electrode's surface from the

30 reinforcing component. Figure 1a of this patent also describes a prior-art identification system ("reader") that can be used to interrogate and power the transponder within the tire. The identification system includes a portable hand-held module having within it an exciter and associated

35 circuitry for indicating to a user the numerical identification of the tire/transponder in response to an interrogation signal.

Typically, in an IC transponder, the IC chip and other components are mounted and/or connected to a substrate such as a printed circuit board (PCB). For example, a pressure transducer may be mounted to the PCB and wired either  
5 directly to the IC chip or indirectly to the IC chip via conductive traces on the PCB. The PCB substrate is suitably a reinforced epoxy laminate having a thickness of twenty mils, and having a glass transition temperature exceeding 175°C (degrees Celsius). A suitable PCB material is available as  
10 "high performance" FR-4 epoxy laminate, grade 65M90, sold by Westinghouse Electric Corporation, Copper Laminates Division, 12840 Bradley Avenue, Sylmar, CA 91342.

There have thus been described, hereinabove, a number of RF transponders suitable for mounting within a pneumatic  
15 tire. The environment within which a tire-mounted transponder must reliably operate, including during manufacture and in use, presents numerous challenges to the successful operation of the transducer. For example, the pressure sensor used with the transponder preferably will have an operating temperature  
20 range of up to 125°C, and should be able to withstand a manufacturing temperature of approximately 177°C. For truck tire applications, the pressure sensor must have an operating pressure range of from about 50 psi (pounds per square inch) to about 120 psi (from about 345 kp (kiloPascals) to about  
25 827 kp), and should be able to withstand pressure during manufacture of the tire of up to about 400 psi (about 2758 kp). The accuracy, including the sum of all contributors to its inaccuracy, should be on the order of plus or minus 3% of full scale. Repeatability and stability of the pressure  
30 signal should fall within a specified accuracy range.

The transponder must therefore be able to operate reliably despite a wide range of pressures and temperatures. Additionally, a tire-mounted transponder must be able to withstand significant mechanical shocks such' as may be  
35 encountered when a vehicle drives over a speed bump or a pothole.

Suitable pressure transducers for use with a tire-

mounted transponder include:

(a) piezoelectric transducers;

(b) piezoresistive devices, such as one of those disclosed in U.S. Patent No. 3,893,228 issued in 1975 to George, et al., and in U.S. Patent No. 4,317,216 issued in 1982 to Gragg, Jr.;

(c) silicon capacitive pressure transducers, such as is disclosed in U.S. Patent No. 4,701,826 issued in 1987 to Mikkor;

(d) devices formed of a variable-conductive laminate of conductance ink; and

(e) devices formed of a variable-conductance elastomeric composition.

#### BRIEF SUMMARY OF THE INVENTION

It is a broad object of the present invention to monitor an ambient temperature in the vicinity of an integrated circuit (IC) chip as defined in one or more of the appended claims and, as such, having the capability of being constructed to accomplish one or more of the following subsidiary objects.

It is a broad object of the invention to monitor an ambient temperature in the vicinity of an integrated circuit (IC) chip, the IC chip having functionality other than temperature-sensing, such as a radio frequency (RF) transponder ("tag") capable of transmitting data related to a monitored object and parameters associated with the object to an external reader/interrogator.

It is another object of the present invention to provide a technique for utilizing the sensed temperature data, in combination with other sensed parameter data (such as pressure data), to provide a temperature-compensated value for the other sensed parameter data.

It is a further object of the invention to provide an improved radio frequency (RF) transponder ("tag") capable of transmitting data related to a monitored object and parameters associated with the object to an external reader/interrogator.

It is another object of the present invention to provide pressure data from a transponder to an external reader/interrogator in a manner in which temperature-dependency of the pressure data can be eliminated from the pressure data, resulting in a temperature-compensated pressure measurement being displayed by the external reader/interrogator.

According to the invention, a predictable temperature-dependent characteristic voltage of a temperature-sensitive component of an integrated circuit (IC) chip, for example the base-emitter voltage ( $V_{be}$ ) of a lateral bipolar transistor ( $Q1$ ), is superimposed across an external precision resistor ( $R_{ext}$ ). A temperature-dependent current  $I(T)$  is thereby caused to flow through the external resistor ( $R_{ext}$ ). The temperature-dependent current flowing through the external resistor is provided (e.g., mirrored) to another circuit on the IC chip, the output of which is proportional to the temperature-dependent current  $I(T)$  flowing through the resistor. In an embodiment of the invention, the other circuit is a relaxation oscillator, and the output of the other circuit is a temperature-dependent frequency. Inasmuch as the temperature sensor is preferably implemented "on-chip" it should be understood that the IC chip should be a low-power device that generates relatively little internal heat, as contrasted with ambient heat being sensed by the on-chip temperature sensor.

According to an aspect of the invention, the IC chip functions as a radio-frequency (RF) transponder comprising circuitry capable of transmitting information unique to an object with which the transponder is associated to an external reader/interrogator. The temperature-sensitive component (temperature sensor), and one or more additional sensors (transducers) provide real-time parameter measurement at the transducer location. These measurements are transmitted to the external reader/interrogator, in the form of data, in a data stream on a signal which is output by the transponder, such as by impressing (modulating) the data

stream onto a RF signal transmitted by the transponder to the external reader/interrogator.

According to an aspect of the invention, the transponder is preferably powered by an RF signal from the external  
5 reader/interrogator. However, it is within the scope of this invention that the transponder is battery-powered.

According to an aspect of the invention, the transponder is preferably implemented on a single integrated circuit (IC) chip, with a minimum of external instrumentalities such as an  
10 antenna.

According to an aspect of the invention, at least one real-time parameter which is measured is temperature. Preferably, the temperature sensor is embedded ("on-chip") in the IC chip of the transponder.

According to an aspect of the invention, an additional  
15 real-time parameter which may be measured is pressure. Pressure is preferably measured by a separate ("off-chip") pressure sensor, which is preferably of a type that varies its capacitance value as a function of ambient pressure.  
20 Preferably, the temperature sensor is disposed so as to be subject to substantially the same ambient temperature as the pressure sensor so that a true, temperature-compensated pressure can readily be calculated.

According to an aspect of the invention, another  
25 additional parameter which may be measured is in the form of an indication that an excessively high temperature condition, albeit transient, has previously occurred. It should be understood that this parameter is different in nature than the real-time parameters of temperature and pressure. An  
30 example of a sensor suitable for sensing and indicating that such a transient over-temperature condition has occurred can be found in U.S. Patent No. 5,712, 609, issued 27 January 1998 to Mehregany, et al. and incorporated by reference in its entirety herein. Mehregany's sensor is cited as being  
35 exemplary of a suitable Maximum Temperature Measurement Switch (MTMS) for use with the transponder of the present invention. Reference is also made to U.S. Patent No.

5,706,565 which is incorporated in its entirety by reference herein.

The transponder is primarily intended to be associated with a pneumatic tire, and is preferably located within the  
5 tire. However, it is within the scope of this invention that the transponder is associated with another object being monitored, such as an animal.

In a preferred embodiment, the transponder comprises:

- circuitry for receiving an RF signal at a first  
10 frequency ( $F_i$ ) from the external reader/interrogator and processing the received RF signal to provide power and clock pulses to other circuitry;
- circuitry for controlling window(s) of time during which real-time parameter measurement(s) is (are) made, and  
15 captured;
- circuitry for storing calibration constants; and
- circuitry for impressing (preferably by Phase Shift Keying (PSK) modulation) the captured real-time parameter measurements and excessive temperature condition indication  
20 onto a signal which is transmitted back to the external reader/interrogator at a second frequency ( $F_c$ ) which is different from the first frequency ( $F_i$ ).

Other objects, features and advantages of the invention will become apparent in light of the following description  
25 thereof.

#### BRIEF DESCRIPTION OF THE DRAWINGS

Reference will be made in detail to preferred embodiments of the invention, examples of which are illustrated in the accompanying drawings. The drawings are  
30 intended to be illustrative, not limiting.

Certain elements in selected ones of the drawings may be illustrated not-to-scale, for illustrative clarity.

Often, similar elements throughout the drawings may be referred to by similar reference numerals. For example, the  
35 element 199 in a figure (or embodiment) may be similar in many respects to the element 299 in another figure (or

embodiment). Such a relationship, if any, between similar elements in different figures or embodiments will become apparent throughout the specification, including, if applicable, in the claims and abstract.

5 In some cases, similar elements may be referred to with similar numbers in a single drawing. For example, a plurality of elements 199 may be referred to as 199a, 199b, 199c, etc.

10 The cross-sectional views presented herein may be in the form of "slices", or "near-sighted" cross-sectional views, omitting certain background lines which would otherwise be visible in a true cross-sectional view, for illustrative clarity.

15 The structure, operation, and advantages of the present preferred embodiment of the invention will become further apparent upon consideration of the following description taken in conjunction with the accompanying drawings, wherein:

20 **Figure 1** is a generalized block diagram of a RF transponder system comprising an external reader/interrogator and a RF transponder within a pneumatic tire, according to the prior art;

**Figure 2** is a block diagram of major components of a RF transponder, according to the present invention;

25 **Figure 3** is a schematic diagram of major portions of the RF transponder of **Figure 2**, according to the present invention;

**Figure 3A** is a schematic diagram of a portion of the RF transponder of **Figure 2**, according to the invention;

30 **Figure 3B** is a schematic diagram of a portion of the RF transponder of **Figure 2**, according to the invention;

**Figure 3C** is a diagram of a memory space within the RF transponder of **Figure 2**, illustrating how data may be arranged and transmitted, according to the invention; and

35 **Figure 4** is a schematic block diagram of a receiving portion of a reader/interrogator, according to the invention.

DETAILED DESCRIPTION OF THE INVENTION

Figure 1 illustrates a RF transponder system 100 of the prior art, comprising a RF (radio frequency) transponder 102 disposed within (e.g., mounted to an inner surface of) a pneumatic tire 104. An antenna, not shown, is mounted within the tire 104 and is connected to the transponder 102. The transponder 102 is an electronic device, capable of transmitting an RF signal comprising unique identification (ID) information (e.g., its own serial number, or an identifying number of the object with which it is associated -in this example, the tire 104) as well as data indicative of a parameter measurement such as ambient pressure sensed by a sensor (not shown) associated with the transponder 102 to an external reader/ interrogator 106. The external reader/interrogator 106 provides an RF signal for interrogating the transponder 102, and includes a wand 108 having an antenna 110, a display panel 112 for displaying information transmitted by from the transponder 102, and controls (switches, buttons, knobs, etc.) 114 for a user to manipulate the functions of the reader/ interrogator 106. The present invention is directed primarily to implementing the RF transponder. Nevertheless, certain functionality for a reader/interrogator to be compatible with the transponder of the present invention is discussed hereinbelow with respect to **Figure 4**.

As is known, the ID and/or parameter measurement information may be encoded (impressed) in a variety of ways on the signal transmitted by the transponder 102 to the reader/interrogator 106, and subsequently "de-coded" (retrieved) in the reader/interrogator 106 for display to the user. The RF transponder 102 may be "passive", in that it is powered by an RF signal generated by the external reader/interrogator 106 and emitted by the antenna 108. Alternatively, the RF transponder may be "active", in that it is battery-powered. Transponder systems such as the transponder system 100 described herein are well known.

Figure 2 is a block diagram of the RF transponder 200

(compare 102) of the present invention, illustrating the major functional components thereof.

The transponder 200 is preferably implemented on a single integrated circuit (IC) chip shown within the dashed line 202, to which are connected a number of external components. Other dashed lines in the figure indicate major functional "blocks" of the transponder 200, and include a transponder "core" 204 and a sensor interface 206. The components external to the IC chip 202 include an antenna system 210 comprising an antenna 212 and a capacitor 214 connected across the coil 212 to form an L-C resonant tank circuit, an external precision resistor ("R<sub>ext</sub>") 216, an external pressure-sensing capacitor ("C<sub>p</sub>") 218, and an optional external maximum temperature measurement switch ("MTMS") 220. The antenna may be in the form of a coil antenna, a loop antenna, a dipole antenna, and the like. Alternatively, the signal output by the transponder may be provided on a transmission line. In the main hereinafter, a transponder having a coil antenna is described.

The transponder core 204 includes interface circuitry 222 for processing an RF signal, such as a 125 kHz (kilohertz) un-modulated carrier signal received by the antenna 212, for rectifying the received RF signal, and for providing voltages for powering other circuits on the IC chip 202. For example, the interface circuitry provides a regulated supply voltage (V<sub>dd</sub>) of 2.5 volts, and a temperature-independent bandgap voltage (V<sub>bg</sub>) of 1.32 volts. The provision of various supply and reference voltages for the transponder circuitry are described in greater detail hereinbelow, with reference to **Figure 3B**. The interface circuitry 222 also provides the received RF signal, preferably at the frequency (F<sub>i</sub>) it is received, to a clock generator circuit 224 which generates clock signals in a known manner for controlling the timing of other circuits on the IC chip 202 as well as the frequency (F<sub>c</sub>) of a signal which is transmitted by the transponder to the external reader/interrogator.

A timing generator/sequencer circuit 226 receives the clock pulses from the clock generator circuit 224 and processes (e.g., divides) the clock pulses to generate timing windows ( $W_t$  and  $W_p$ , described hereinbelow) for predetermined periods of time during which parameter (e.g., temperature and pressure) measurements are made. The timing windows ( $W_t$  and  $W_p$ ) may either be of substantially equal duration or of unequal duration. The timing generator/sequencer circuit 226 also controls the timing and sequence of various functions (e.g., pressure measurement and capture, temperature measurement and capture, described in greater detail hereinbelow) performed in the sensor interface 206, and is preferably implemented as an algorithmic state machine (ASM).

The transponder core 204 further includes a register/counter circuit 230 which includes a temperature register 232 (e.g., 12-bit) and a pressure register 234 (e.g., 12-bit) for capturing and storing temperature and pressure measurements (counts), respectively, and a block 236 of addressable memory, which includes an EEPROM array. The registers 232 and 234 and EEPROM array 236 are shown in a dashed line 238 representing a block of addressable memory on the IC chip.

The register/counter circuit 230 also includes a multiplexer and column decoder 240, as well as a row decoder 242 for controlling the sequence in which signals (i.e., data) are output on a line 244 to a modulation circuit 246 which, via the interface circuitry 222, communicates selected measured tire-operating characteristics in a data stream via the antenna interface 210 to the external reader/interrogator (106, Figure 1).

The transponder core 204 also includes a baud rate generator 248 which controls the rate at which modulating information (e.g., the temperature or pressure measurement) is applied to the modulation circuit 246. The baud rate generator 248 also provides a data carrier clock controlling the output frequency ( $F_c$ ) of the transponder and a data rate

clock controlling a rate at which the data stream including measurements, calibration information, etc. is modulated onto the transponder output carrier.

5 The sensor interface 206 includes a circuit 250 for generating an output current  $I(T)$  on a line 251 which is related to a predictable characteristic voltage of a temperature-sensitive component (e.g.,  $V_{be}$  of a transistor  $Q1$ , described hereinbelow) which is superimposed on the external resistor ( $R_{ext}$ ) 216. The output current  $I(T)$  on the  
10 line 251 is provided to a current steering circuit 252 and to a relaxation oscillator 254. In general terms, the relaxation oscillator 254 oscillates at a frequency controlled by a rate of voltage change ( $dV/dT$ ) produced on an output line 253 from the current steering circuit 252. The  
15 rate of voltage change on the line 253 is a function of the output current  $I(T)$  on line 251 and of internal capacitances ( $C_{rx}$ ) associated with the relaxation oscillator as well as an external capacitance ( $C_p$ ) that can be switched into the oscillator circuit. An output signal from the relaxation  
20 oscillator 254 is provided on a line 255 which, as will be explained in greater detail hereinbelow, is indicative of both ambient temperature and ambient pressure. As used herein, the term "ambient" refers to the parameter being measured in the vicinity of the transponder, more  
25 particularly the respective sensors associated with the transponder. When the transponder is mounted within a pneumatic tire, "ambient pressure" refers to the pressure within the tire.

In operation, an RF signal from an external source  
30 (i.e., reader/interrogator, not shown, compare 106, **Figure 1**) is received by the antenna 212. This RF signal is rectified and used to power the RF transponder 200. Modulating information applied to the modulation circuit 236 is used to alter characteristics of the antenna interface (e.g.,  
35 impedance, resonant frequency, etc.). These alterations are sensed by the external reader/interrogator and are decoded, providing communication of temperature and pressure

information back from the RF transponder 200 to the external reader/interrogator.

The timing generator/sequencer circuit 226 controls whether the current  $I(T)$  on the line 251 is "steered" into one or the other of two capacitors ( $C_{FX1}$  or  $C_{FX2}$ , described hereinbelow with respect to the relaxation oscillator 312) associated with the relaxation oscillator 254, and whether the external pressure-sensing capacitance ( $C_p$ ) 218 is or is not included in the generation of an output signal ( $F_{osc}$ ) by the relaxation oscillator 254. For example, to measure temperature, the current  $I(T)$  is steered into the internal oscillator capacitors ( $C_{FX}$ ), but the pressure-sensing capacitor ( $C_p$ ) is disconnected from (not included in) those capacitances. This means that the frequency of the oscillator output signal seen on line 255 is a function of temperature alone. When the pressure-sensing capacitor ( $C_p$ ) 218 is "switched in", then the output frequency of the oscillator 254 on the line 255 will, as explained in greater detail hereinbelow, be a function of both pressure and temperature. As described in greater detail hereinbelow, an algorithm is employed in the reader/interrogator to generate a temperature-independent measurement of pressure.

As controlled by the timing generator/sequencer circuit 226, either the 12-bit temperature register 232 or the 12-bit pressure register 234 (depending upon whether temperature or pressure is being measured) counts (captures) oscillations of the oscillator output signal on line 255. (Counters, not shown, are associated with these "registers.") The timing "window" provided by the timing generator/sequencer circuit 226 has a known, controlled duration. As a result, the count remaining in (captured by) the respective temperature or pressure counter (register) when the timing window "closes" is a function of (proportional to) the oscillation frequency ( $F_{osc}$ ) of the relaxation oscillator 254, and therefore a function of temperature or pressure, whichever is being measured.

The EEPROM array 236 is used to hold calibration constants that the reader system uses to convert temperature and pressure counts ( $N_t$  and  $N_p$ , respectively, described in greater detail hereinbelow) into temperature and pressure readings which can be displayed (e.g., via display 112) to a user. The EEPROM array 236 can also store the ID of the transponder, calibration data for the transponder, and other data particular to the given transponder.

Figure 3 is a more-detailed schematic diagram 300 of several of the components of the transponder 200 of Figure 2, primarily those components described hereinabove with respect to the sensor interface section 206 of Figure 2.

In this schematic diagram 300, conventional circuit symbols are employed. For example, lines which cross over one another are not connected to one another, unless there is a "dot" at their junction (cross-over), in which case the lines are connected with one another. Conventional symbols are employed for transistors, diodes, ground connections, resistors, capacitors, switches, comparators, inverters, and logic gates (e.g., "AND", "NAND", "OR", "NOR").

The circuit is described in terms of a CMOS embodiment, wherein "P" (e.g., "P1") indicates a PMOS (P-channel) transistor and "N" (e.g., "N1") indicates an NMOS (N-channel) transistor. CMOS transistors are of the FET (field effect transistor) type, each having three "nodes" or "terminals" - namely, a "source" (S), a "drain" (D), and a "gate" (G) controlling the flow of current between the source and the drain. In the description that follows, it will be evident that a number of the PMOS and NMOS transistors are "diode-connected", meaning that their drain (D) is connected to their gate (G). The general theory of operation of transistors, particularly CMOS transistors, is well-known to those having ordinary skill in the art to which the present invention most nearly pertains.

As will evident from the description that follows, a number of the CMOS transistors are connected in a "current-mirroring" configuration. The concept of current-mirroring

is well known, and in its simplest form comprises two similar polarity transistors (e.g., two PMOS transistors) having their gates connected with one another, and one of the pair of transistors being diode-connected. Current-mirroring generally involves causing a current to flow through the diode-connected transistor, which results in a gate voltage on the diode-connected transistor required to produce that current. Generally, the gate voltage of the diode-connected transistor is forced to become whatever voltage is necessary to produce the mirrored current through that transistor. Since the diode-connected transistor, by definition, has no gate current, by applying the gate voltage of the diode-connected transistor to any other identically-connected transistor, a mirrored-current will flow through the identically-connected transistor. Typically, the current-mirroring transistors all have the same physical area, in which case the mirrored current will be essentially same as the current which is being mirrored. It is also known to produce a mirrored current which is either greater than or less than the current being mirrored by making one of the transistors physically larger or smaller (in area) than the other. When such identically-connected transistors having different areas are connected in a current-mirroring configuration, their scaled (larger or smaller) areas will produce correspondingly scaled (larger or smaller) currents.

In the main hereinafter, the numerous connections between the various components of the circuit are clearly illustrated in the figure, and the descriptive emphasis is on the various functions of and interactions between the various components of the circuit rather than on reciting (ad nauseam) each and every individual connection between the various components, all of which are explicitly illustrated in the figure.

The antenna system 210 comprises a coil antenna 212 and a capacitor 214 connected across the antenna 212 to form an L-C resonant tank circuit providing an alternating current (AC) output to a full-wave rectifier circuit 302.

The full-wave rectifier circuit 302 comprises two PMOS transistors and two diodes, connected in a conventional manner, as shown, and outputs a full wave rectified direct current (DC) voltage on a line 303. A capacitor 304 is  
5 connected between the line 303 and ground to "smooth out" (filter) variations ("ripple") in the full wave rectified DC voltage on the line 303. The voltage on the line 303 thus becomes a usable voltage for the remaining components of the transponder - in this case, a positive supply voltage (Vcc)  
10 on the line 303.

A temperature-sensing circuit 306, corresponding approximately to the base-emitter voltage-to-current converter 250 of **Figure 2**, is connected between the line 303 (Vcc) and ground, and includes four CMOS transistors labeled  
15 P1, P2, N1 and N2 and a lateral bipolar transistor labeled Q1, and is connected to the external resistor 216 (Rext). The transistors P2 and N1 are diode-connected, as illustrated. The two transistors P1 and P2 are connected in a current-mirroring configuration, and the two transistors N1  
20 and N2 are also connected in what can generally be considered to be a current-mirroring configuration. The source of the transistor N1 is connected via the transistor Q1 to ground, and the source of the transistor N2 is connected via a the external resistor (Rext) 216 to ground.

As will become evident, the ability of the temperature-sensing circuit 306 to produce a signal (i.e., a current) that is proportional to a sensed (ambient) temperature (e.g., within the tire with which the transponder is associated) is largely dependent on the characteristic that the base-emitter  
30 voltage of the transistor Q1 is a highly predictable and repeatable function of temperature. The resistor (Rext) 216 is an external, precision, reference resistor, whose value is substantially independent of temperature (as contrasted with the temperature dependency of the transistor Q1). A suitable  
35 value for the resistor (Rext) 216 is 20.5 kΩ.

The transistor N2 is connected between the transistor P2 and the external resistor 216 ( $R_{ext}$ ) in a "source-follower" mode. As a voltage is impressed on the gate of the transistor N2, its source voltage will "follow" its gate voltage (minus an inherent voltage drop ( $V_{gs}$ ) between its gate and its source).

As current flows through the transistor N1, its gate voltage will be offset by its gate-source voltage drop ( $V_{gs}$ ) above the emitter voltage at the transistor Q1. Since the transistors N1 and N2 are essentially identical, with the same current flowing through each of the two transistors N1 and N2, they will have identical gate-source voltage drops ( $V_{gs}$ ). As a result, the voltage at the source of the transistor N2 across the external resistor 216 ( $R_{ext}$ ) will be essentially identical to the voltage at the emitter of the transistor Q1. Hence, applying Ohm's law ( $E=IR$ , or  $I=E/R$ ), the current through the external resistor 216 ( $R_{ext}$ ) will equal the emitter voltage of the transistor Q1 divided by the resistance of the external resistor 216 ( $R_{ext}$ ).

In normal operation, all of the current flowing through the external resistor ( $R_{ext}$ ) 216 flows through the source of the transistor N2 and, consequently, through the diode-connected transistor P2. By a current-mirroring connection, the current through the transistor P2 is replicated (mirrored) in the transistor P1 and is further replicated (mirrored) in the transistor P4. This ensures that the current flowing through the transistors N1 and N2 will be the same, at all times, which further helps to ensure that the emitter voltage at the transistor Q1 and the voltage across the external resistor ( $R_{ext}$ ) 216 are identical, independent of voltage and process variations. As mentioned hereinabove, the transistors N1 and N2 are connected in what can generally be considered to be a current-mirroring configuration. However, since they are not strictly identically connected, their function in the circuit 306 is

principally for "matching" Q1 and Rext.

In essence, the circuit 306 ensures that the current I(T) flowing through the external resistor (Rext) is predictable, and is a function of the absolute temperature (T) of the transistor Q1. As described in greater detail hereinbelow, this temperature-dependent current I(T) flowing through the external resistor (Rext) 216 is mirrored to a relaxation oscillator (312, described hereinbelow) to provide a signal indicative of the temperature of the transistor Q1 to the external reader (106, Figure 1). As described in greater detail hereinbelow, the output frequency (Fosc) of the relaxation oscillator 312 will be a function of the absolute temperature (T) of the transistor Q1.

At this point, it is useful to note that it is essentially the transistor Q1 that is being employed as the temperature-sensing element of the overall transponder circuit. The transponder circuit advantageously employs an inherent characteristic of such a transistor implemented in CMOS technology that the base-emitter voltage of the transistor Q1 will vary by a predictable amount of -2.2 mV/°C (millivolts per degree Celsius).

It should be noted that the transponder of the present invention is described in terms of a "passive" device, relying on RF energy being supplied to it by an external source (106, Figure 1) to power up its circuitry. However, it is within the scope of this invention that the transponder contain its own power supply, such as in the form of a battery. In either case, when first powering up circuitry such as described with respect to the temperature-sensing circuit 306, it is important to ensure that they "ramp up" to their normal operating state from their quiescent state in a reliable and predictable (controlled) manner. To this end, two lines 305 and 307 are illustrated which are connected between the temperature-sensing circuit 306 and a "startup" circuit 308.

The startup circuit 308 is connected between the supply

voltage (Vcc) on the line 303 and ground, and serves two main purposes: (i) to get current flowing in the temperature-sensing circuit 306 when the transponder (200) first starts up from a powered down state; and (ii) to mirror and convert the current flowing through the transistor P2 from a supply-referenced current to a ground-referenced current.

Startup is initiated by the transistor P3. The transistor P3 is fabricated to have high channel resistance so as to function in a "weak pull-up" mode. With its gate connected to ground, it will always be "on", and will behave essentially like a resistor having a fairly high resistance (e.g., >10k ohms).

Since, at startup, no current flows elsewhere in the circuit, the transistor P3 operates to pull the gate of the transistor N3 towards the supply voltage (Vcc), thereby turning the transistor N3 "on", which effectively connects the transistor's N3 source to its drain which, in turn, causes current to flow through the diode-connected transistor P2 of the temperature-sensing 306 into the drain of the transistor N3. This causes the voltage at the source of the transistor P2 to decrease, thereby causing current to flow in the transistors P1 and P4. As current flows through the transistor P4 into the diode-connected transistor N5, a current-mirroring connection between the transistors N4 and N5 causes a corresponding current to flow through the transistor N4, thereby pulling the gate of transistor N3 to ground, thereby effectively shutting "off" the flow of current through the transistor N3.

However, with current now flowing through the current-mirrored transistors P1, P2 and P4, current flowing from the transistor P1 through the transistor N1 into the transistor Q1 forces the temperature-sensing circuit 306 to "start up" in its stable operating point state (rather than its zero current state).

After startup, the transistor N3 essentially "drops out" of

the circuit, having performed its intended function.

The transistor N5 is connected in a current-mirroring configuration with the transistor N4 (and, as described hereinbelow, with the transistor N6). Therefore, essentially, with a current equivalent to the current through the external resistor (R<sub>ext</sub>) 216 flowing through the transistor N5, the same current flows through the transistor N4, thereby establishing a reference voltage (N<sub>bias</sub>) on the line 309. The reference voltage (N<sub>bias</sub>) on the line 309, as well as a supply voltage (V<sub>dd</sub>) on a line 309', are provided to a current-scaling circuit 310.

The supply voltage (V<sub>dd</sub>) on the line 309' is provided in any suitable manner, such as a multiple of a bandgap voltage (V<sub>bg</sub>) generated in a conventional manner elsewhere on the chip, and its magnitude (e.g., 1.32 volts) should be independent of temperature, such as inherent to the silicon process which is employed in making the chip. The provision of such a stable (e.g., bandgap) voltage (e.g., V<sub>bg</sub>) and the supply voltage (e.g., V<sub>dd</sub>) derived therefrom is well within the purview of one having ordinary skill in the art to which the present invention most nearly pertains, and is described in greater detail hereinbelow with respect to Figure 3B.

The current-scaling circuit 310 is constructed in the following exemplary manner. The sources of the transistors P5 and P6 are connected to supply voltage V<sub>dd</sub>. The gate of a transistor N6 receives the reference voltage (N<sub>bias</sub>) on the line 309. The transistor N6 is connected in a current-mirroring configuration with the transistor N5 (as well as with the aforementioned transistor N4) and will therefore mirror the flow of current I(T) through the transistors N4 and N5. Consequently, the flow of current through the diode-connected transistor P5 will mirror the flow of current through the transistors N4, N5 and N6.

The transistors P5 and P6 are connected in a current-mirroring configuration, but are fabricated (using

conventional CMOS fabrication techniques) such that current flowing through the transistor P6 is scaled up or down by a ratio (N) of the physical area of the transistor P5 to the physical area of the transistor P6. For example, if the  
5 transistor P6 is smaller in size than the transistor P5 (i.e., the transistor P5 is "N" times larger in area than the transistor P6), then the current flowing through the transistor P6 will be commensurately (N times) smaller than the current flowing through the transistor P5. Thus, the  
10 "scaled" current flowing through the transistor P6, is labeled " $I(T)/N$ " in the figure, and is provided on a line 311 to a relaxation oscillator circuit 312. It is well known that the ratio of the currents between the transistors P5 and P6 can readily be established by conventional circuit  
15 processing techniques, such as by simply making one of the transistors larger than the other, or by implementing a one of the two transistors as the aggregate of two or more same-size transistors so that their aggregate area is larger than the area of the other of the two transistors.

20 The relaxation oscillator circuit 312 is of fairly conventional design, and includes two pair of transistors at the "front end" of each of its two phase paths - a pair of complementary transistors P7 and N7 at the front end of a one phase path ( $\phi 1$ ) 314a, and another pair of complementary  
25 transistors P8 and N8 at the front end of another phase path ( $\phi 2$ ) 314b.

Connected as illustrated, for a given pair of transistors (e.g., P7 and N7), when with their common gate voltage is high (i.e., towards positive supply) their output  
30 will be grounded, and when their common gate voltage is low they will provide the current  $I(T)/N$  flowing on the line 311 to a respective one of the phase paths (e.g., 314a) of the relaxation oscillator 312. As is known, in such an arrangement, when the common gate voltage of a one of the  
35 pairs of transistors (e.g., P7 and N7) is high, the common

gate voltage of the other of the pairs of transistors (e.g., P8 and N8) will be low, and vice-versa. In this manner, each phase path 314a and 314b has a duty cycle (i.e., its "on" time), which may be the same as or may be different than the  
 5 duty cycle of the other phase path 314b and 314a, respectively. Thus, each pair of transistors (e.g., P7 and N7) may be considered to be an "input switch" to its respective phase path (e.g., 314a).

Each phase path 314a and 314b of the relaxation  
 10 oscillator 312 has a comparator 316a and 316b, respectively, at its input, and has a fixed-value capacitor  $C_{fx1}$  and  $C_{fx2}$ , respectively, connected between the negative (-) input of the comparators 316a and 316b and ground. The capacitors  $C_{fx1}$  and  $C_{fx2}$  have exemplary capacitance values of 2-5 pf (picofarads)  
 15 and 2-5 pf, respectively, and are preferably implemented as "on-chip" devices, such as poly-to-poly capacitors exhibiting a low temperature coefficient (e.g., less than 20ppm). The positive (+) inputs (terminals) of the comparators 316a and 316b are tied together and are set to a reference threshold  
 20 voltage  $V_{bg}$ , such as 1.32 volts, which is independent of temperature.

A "NOR" logic gate 318a and 318b is connected at the output of each phase path 314a and 314b, respectively, and the two NOR gates 318a and 318b are cross-connected to form a  
 25 latching circuit having an output on a line 319. The cross-connected NOR gates 318a and 318b are thus capable of functioning as a flip flop, or an RS (re-set/set) latch.

When the common gate voltage of one of the input switches (e.g., P7 and N7) is high, the respective capacitor  
 30 (e.g.,  $C_{fx1}$ ) for that phase path (e.g., 314a) is grounded (shorted out, caused to be devoid of charge). Conversely, when the common gate voltage of one of the input switches (e.g., P7 and N7) is high, the scaled current  $I(T)/N$  is applied to (allowed to flow into) the respective capacitor  
 35 (e.g.,  $C_{fx1}$ ) for that phase path (e.g., 314a), and the capacitor and it begins to charge (acquire an increasing

voltage across the capacitor). When the voltage across the capacitor reaches the comparator reference voltage (e.g., 1.32 volts) the output of the comparator goes low and changes the state of the output of the latch 318a/318b on the line 319. In this manner, the relaxation oscillator will oscillate at a frequency ( $F_{osc}$ ) determined by the rise time of the capacitors  $C_{FX1}$  and  $C_{FX2}$  and, importantly, by the scaled current  $I(T)/N$  being supplied to the capacitors  $C_{FX1}$  and  $C_{FX2}$ . With greater current  $I(T)/N$  being supplied, the voltages of the capacitors  $C_{FX1}$  and  $C_{FX2}$  will rise faster, crossing the threshold voltage faster, and causing the relaxation oscillator 312 to oscillate faster, thereby increasing the frequency of the signal  $F_{osc}$  on the line 319. The signal  $F_{osc}$  on the line 319 is inverted by an inverter 320, as shown, to provide a signal  $F_{osc}'$  on the line 321.

As described in greater detail hereinbelow, the oscillator 312 is controlled to run in two mutually-exclusive modes, a temperature-sensing mode (between times  $t_0$  and  $t_1$ ) and a pressure-sensing mode (between times  $t_1$  and  $t_2$ ), as controlled by the timing generator/sequencer 226. The frequency of the oscillator output signal  $F_{osc}$  (and of  $F_{osc}'$ ) will be different in each of these two modes.

#### GENERATING TEMPERATURE AND PRESSURE SIGNALS

In the exemplary context of the transponder 200 being associated with a pneumatic tire, it is principally desirable to determine the pressure within the pneumatic tire. For example, a typical passenger vehicle tire may be properly inflated at about 32 psi (about 221 kp).

It is, for example, estimated that an approximate 10% decrease in fuel consumption could be realized if the pneumatic tires on vehicles were operated at their specified pressure. Although vehicle fleet operators are typically sensitive to this issue, and check and adjust tire pressure frequently, the average operator of a passenger vehicle is often less inclined to keep an eye on their tire pressure until, for example, the tire is visibly flattened out. In

such cases, an LCD (liquid crystal display) readout or the like on the dashboard of a car could provide dynamic tire inflation information to the operator of a vehicle, the pneumatic tires of which are equipped with a transponder such as the one described herein. Of no less significance is the emergence of "run-flat" tires being marketed by various tire manufacturers. The Goodyear EMT (extended mobility tire) series of tires is an example of a run-flat tire, an overall purpose of which is to allow a driver to travel up to 50 miles ( $\approx 120$  kilometers) on a deflated tire, at "reasonable" operating speeds (e.g., 60 miles per hour, or 144 kilometers per hour), while maintaining normal control over the vehicle. Such run-flat tires are generally well known, and do not form a portion of the present invention, per se. When running flat on a run-flat tire, it is particularly important that the driver be alerted to the fact that he or she is operating the vehicle on "borrowed time" as indicated, principally, by an indication, whether visual or audio (e.g., a beep) that the tire is indeed flat and needs to be repaired or replaced at his or her earliest convenience.

By allowing the relaxation oscillator 312 to run, the frequency of its output signal  $F_{osc}$  (and  $F_{osc}'$ ) will be a function of the absolute temperature of (sensed by) the transistor Q1. This is true in both the temperature-sensing mode and the pressure-sensing mode of operation.

In the temperature-sensing mode, and in the case that the capacitance values for  $C_{fx1}$  and  $C_{fx2}$  are equal, which is preferred, the relaxation oscillator 312 will have a symmetrical (balanced, 50%) duty cycle. In the pressure-sensing mode, the pressure-sensing capacitor ( $C_p$ ) 218 is switched by a semiconductor switch 350 across  $C_{fx2}$ , which changes the duty cycle and output frequency  $F_{osc}$  (and  $F_{osc}'$ ) of the relaxation oscillator.

In the temperature-sensing mode, only the fixed capacitors  $C_{fx1}$  and  $C_{fx2}$  are being alternately charged (and discharged) resulting in a 50% duty cycle with a period

proportional to ambient temperature. In the pressure-sensing mode, the pressure-sensing capacitor ( $C_p$ ) 218 is switched into phase path 314b of the oscillator 312. Thus, for a given temperature, for the first half of the oscillator period the phase path 314a behaves in the same manner as in the temperature-sensing mode, and for the second half of the oscillator period the phase path 314b behaves in a manner that is proportional to the capacitance value of the fixed capacitor  $C_{fx2}$  plus the capacitance value of the pressure-sensing capacitor ( $C_p$ ) 218. This, in effect, slows down the oscillator and changes its duty cycle. The change in the duty cycle is indicative of the ratio of  $C_p$  to  $C_{fx2}$ . Thus, from the ratio of the two periods (with and without  $C_p$  in the circuit, it is straightforward to calculate what the additional capacitance  $C_p$  is, hence the sensed pressure. As described in greater detail hereinbelow, the temperature-dependency of the oscillator output in the pressure-sensing mode can be completely eliminated, in a straightforward manner.

The "slowing down" of the oscillator when the pressure-sensing capacitor ( $C_p$ ) 218 is switched into the oscillator circuit results, inevitably, in there being relatively fewer oscillator output pulses (reduced output frequency) to count during a given pressure-measurement window (e.g.,  $W_p$ ) than during a similar- duration temperature-measurement window (e.g.,  $W_t$ ). In other words, a "slowed-down" oscillator will reduce that rate at which counts indicative of the parameter measurement are collected. In order to increase the resolution (quantity) of the counts ( $N_p$ ) generated during the pressure-measurement window ( $W_p$ ), it is contemplated that the pressure-measurement window ( $W_p$ ) can be increased in size (changed in duration) so as to allow for the capture of an appropriate number of pressure counts in the pressure register 234. This can readily be accomplished simply by establishing a larger (than otherwise) value for the time  $t_2$  which establishes the end of the pressure-measurement window

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( $W_p$ ) in the pressure-sensing mode (between times  $t_1$  and  $t_2$ ), as controlled by the timing generator/sequencer 226. For example, the temperature-measurement window  $W_T$  (between times  $t_0$  and  $t_1$ ) can be on the order of several ones (e.g., eight) of milliseconds, and the pressure-measurement window  $W_p$  can be on the order of tens or dozens (e.g., forty) of milliseconds. Alternatively, it is contemplated that the scaled current ( $I(T)/N$ ) flowing out of the current-scaling circuit 310 to the relaxation oscillator 312 could be increased during the pressure-measurement window ( $W_p$ ) to increase the fundamental frequency of the relaxation oscillator 312, thereby increasing the overall resolution of the pressure count. This can readily be accomplished, for example in the case of P6 being smaller in size (area) than the transistor P5, simply by switching in a transistor P6' (not shown) in lieu of the transistor P6, the transistor P6' having a larger area than the transistor P6 so that the ratio of the areas of the transistors P5 and P6 is closer to unity (i.e., less scaled down) and the current to the relaxation oscillator 312, hence its counting rate, is increased. Such switching in of another transistor P6' is readily effected with a switch (not shown) comparable to the aforementioned switch 350 which switches in the pressure-sensing capacitor ( $C_p$ ) 218. One having ordinary skill in the art to which the present invention most nearly pertains will readily understand how to offset the "slowing down" of the oscillator when the pressure-sensing capacitor ( $C_p$ ) 218 is switched into the oscillator circuit, in light of the teachings presented herein.

### 30 MEASURING PARAMETERS

When the transponder is powered up, temperature and pressure are continuously measured, and these measurements are transmitted back to the external reader/interrogator (106) as data words in a data stream. For example, each of the temperature and pressure parameters can be transmitted back to the reader/interrogator (106) as 12-bit data words as

selected (known) portions of a larger (e.g., 144-bit) data stream. One bit in the overall data stream may be dedicated to the state (e.g., "closed" or "open") of the MTMS switch (220). A complete description of an exemplary data stream being transmitted by the transponder to the external reader/interrogator is set forth hereinbelow with reference to Figure 3C.

Temperature is suitably measured by counting the number of cycles output from the oscillator 312 during a fixed time period (window of time from  $t_0$  to  $t_1$ ) with a period  $T_w$ . For example, a down-counter (associated with the temperature register (232)) may be clocked by the oscillator, such that at the end of the window  $W_T$ , a temperature count  $N_T$  is generated. The relationship between  $N_T$  and temperature is linear.

#### OPTIMIZING PRESSURE-RESPONSIVENESS

Obtaining (and displaying) an accurate pressure reading being of paramount importance when monitoring the pressure of a pneumatic tire, certain parameters of the transponder circuit may be established to maximize its pressure-responsiveness and therefore improve the accuracy of the pressure reading displayed by the external reader/interrogator (106).

As described hereinabove, the transponder responds to the changing capacitance of the pressure sensor ( $C_p$ ) 218 by changing the value of a binary 12-bit word that is transmitted to the external reader/interrogator (106). This binary word is the count of an oscillator frequency during a timing window  $W_p$  (between  $t_1$  and  $t_2$ ) established by the timing generator/sequencer 226. The pressure response can therefore be described as the change in counts per unit change in capacitance of the pressure-sensing capacitor ( $C_p$ ) 218.

Pressure-responsiveness of the transponder has been found to be dependent on a number of factors, each of which can be analyzed. For example, it has been determined that:

(a) increasing the scaled current  $I(T)/N$  to the oscillator 312 will proportionally increase the pressure

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counts  $N_p$  for a given value of the pressure-sensing capacitor ( $C_p$ ) 218; and

(b) decreasing the values for  $C_{FX1}$  and  $C_{FX2}$  will proportionally increase the pressure counts  $N_p$  for a given value of the pressure-sensing capacitor ( $C_p$ ) 218; and

(c) increasing the current  $I(T)/N$  to the oscillator will proportionally increase the pressure counts  $N_p$  (for a given value of  $C_p$ ) at a greater rate than decreasing the values for  $C_{FX1}$  and  $C_{FX2}$ .

As a general proposition, increasing the pressure counts  $N_p$  is desirable. However, one having ordinary skill in the art to which the present invention most nearly pertains will readily appreciate that there is a practical upper limit to increasing the pressure counts at a frequency which may become unacceptably large for the capability of certain circuits of the IC chip.

#### OBTAINING A PRESSURE READING AT THE READER/INTERROGATOR

The fundamental frequency of the oscillator 312 is set by parameters in the IC chip (e.g., 204) and, as described hereinabove, is temperature-dependent. Therefore, the pressure-response is a function (hybrid) of both temperature and pressure, and the relationship of  $N_p$  to  $C_p$  is nonlinear. Therefore, using a linear equation for calculating the pressure response would inevitably lead to significant errors over a range of pressures being measured. (For limited ranges of pressures being measured, for example over a 20 psi (138 kp) range of pressures, using a linear equation may, however, be acceptable.)

An important advantage of using the transponder circuitry described hereinabove is that the relationship between  $N_T/N_p$  to pressure sensor capacitance is linear, and requires no temperature compensation term in the equation (algorithm) used by the reader/interrogator (106) to calculate pressure, thereby greatly simplifying the design of the reader/interrogator. This beneficial "ratiometric" relationship is readily demonstrated by the following

equations:

$$\text{(eqn. 1) } N_T = T_w * I(t) / (2 * V_{bg} * C_{FX})$$

$$\text{(eqn. 2) } N_p = T_w * I(t) / (V_{bg} * (2 * C_{FX} + C_p))$$

solving for  $N_T/N_p$ , the following is arrived at:

$$\text{5 (eqn. 3) } N_T/N_p = 1 + (C_p / 2 * C_{FX})$$

It can thus be observed that the ratio  $N_T/N_p$  is only a function of  $C_p$  and  $C_{FX}$ , and no other variables. This means that  $N_T/N_p$  is only a function of pressure, and is insensitive to temperature or charging current variations.

10 **Figure 3A** illustrates the components involved in the final step of capturing temperature and pressure measurements in the transponder. The signal **Fosc'** output by the relaxation oscillator 312 is provided to an input of each of two AND gates 360 and 362. A signal ("Capture Temp") is  
 15 provided by the timing generator/sequencer 226 to the other input of the AND gate 360 during the temperature-sensing window ( $W_T$ ) so as to load the temperature register/counter 232 with the count (data)  $N_T$  indicative of measured temperature. Another data signal ("Capture Press") is provided by the  
 20 timing generator/sequencer 226 to the other input of the AND gate 362 during the pressure-sensing window ( $W_T$ ) so as to load the pressure register/counter 234 with the count (data)  $N_p$  indicative of measured pressure. These signals are then shifted out of the registers 232 and 234, via the MUX 240, to  
 25 the modulation circuit 246 described hereinabove.

#### GENERATING RELIABLE SUPPLY AND REFERENCE VOLTAGES

As described hereinabove, the positive (+) inputs (terminals) of the comparators 316a and 316b are tied together and are set to a reference "bandgap" voltage  $V_{bg}$ ,  
 30 such as 1.32 volts, which is independent of temperature. As also mentioned hereinabove, the supply voltage ( $V_{dd}$ ) on the line 309' may be provided as a multiple of the reference bandgap voltage ( $V_{bg}$ ) so as to be a stable operating voltage for the current steering circuit 310 and the relaxation  
 35 oscillator 312.

**Figure 3B** illustrates a circuit 370 suitable for

generating supply voltage  $V_{dd}$ . A temperature-independent calculable bandgap voltage  $V_{bg}$  is readily derived, based on the processing techniques employed in fabricating the IC chip, as being inherent to the selected process (e.g., CMOS).  
5 This bandgap voltage  $V_{bg}$  is provided to the "+" input of an operational amplifier 372, connected as shown, in a feedback loop having gain, to provide supply voltage  $V_{dd}$  as an integral multiple of the bandgap voltage  $V_{bg}$ .

#### AN EXEMPLARY DATA STREAM

10 As mentioned hereinabove, information (data) from the transponder is transmitted to the external reader/interrogator in the form of a data stream, a portion of which is the temperature count  $N_T$ , another portion of which is the pressure count  $N_p$ , and another portion of which  
15 represents the state (e.g., "closed" or "open") of the MTMS switch (220). Remaining portions of the data stream may contain information which is personalized to a given transponder unit such as its ID information (e.g., serial number), calibration constants, and the like.

20 **Figure 3C** illustrates an exemplary architecture for information which is stored (in memory) within the transponder, as well as a data stream which is transmitted by the transponder to the external reader/interrogator. The memory of the transponder core 204 has, for example, a 144-  
25 bit address space which includes 119 (one hundred nineteen) bits of programmable memory and one address location dedicated to the state of the MTMS switch 220, these 120 (one hundred twenty) bits of programmable memory constituting the EEPROM (136), plus the two 12-bit registers 232 and 234.

30 Each of the 119 programmable memory bits can separately be written to with any combination of data, including synchronization (sync) pattern information, general data, error checking codes, and temperature and pressure calibration data. The EEPROM is 'block writeable', meaning  
35 that in the 'write' mode, the entire 120 bits of EEPROM are programmed to a logical (binary) value of "1". Individual bits can be 'erased', or set to a logical value of "0" simply

by clocking the chip to its physical address and placing the chip into the 'erase' mode. The address location is preserved.

In this example, the first twelve data locations  
5 (000..011) in ROW 1 are reserved for sync. The next seventy  
one data locations (012..082) in ROWs 2 through 7 are for  
general information and a value for a data validation  
algorithm such as CRC (Cyclic Redundancy Check). The next  
10 data location (083) contains the logic level (state) of the  
MTMS switch 220. A logical value of "1" indicates that the  
MTMS switch is open and a logical value of "0" indicates that  
the MTMS switch is closed.

The transponder unit is suitably calibrated prior to its  
installation in a tire. This basically involves determining  
15 slope and intercepts for temperature and pressure values  
generated by the transponder at various temperatures and  
pressures in a test chamber, and programming these  
characteristic calibration values associated with the  
transponder into the memory space. The next twelve data  
20 locations (084..095) in ROW 8 hold temperature calibration  
(e.g., intercept) data ("TEMP COMP"). The next twelve data  
locations (096..107) in ROW 9 hold pressure calibration  
(e.g., intercept) data ("PRESS COMP"). The next twelve data  
locations (108..113 and 114..119) in ROW 10 hold calibration  
25 slope information for temperature and pressure, respectively.

According to an aspect of the invention, it has been  
determined that characteristic values for the slope of the  
 $N_T/N_p$ , or "ratioed" response of temperature count divided by  
pressure count, is linear with respect to the value of the  
30 pressure-sensing capacitor  $C_p$ , and using this ratioed value of  
 $N_T/N_p$  requires no temperature compensation term in an equation  
used to calculate pressure. Additionally, it has been  
determined that the ratioed value of  $N_T/N_p$  is less sensitive  
to variations in coupling between the reader/interrogator and  
35 the transponder than either of these measurements taken  
alone. Thus, by determining (during calibration) and storing  
calibration data for the ratioed value of  $N_T/N_p$  in the

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transponder, the ability to determine a true pressure reading which is relatively insensitive to coupling variations between the reader/interrogator and the transponder is both simplified and made more reliable. This ratioed calibration value for  $N_T/N_p$  is stored in the transponder memory and included in the data stream transmitted to the external reader/interrogator.

As counts  $N_T$  and  $N_p$  for temperature and pressure are generated, as described hereinabove, they are stored in ROWs 11 and 12 of the overall memory space, which correspond to the temperature and pressure registers 312 and 314, respectively. Various predetermined values can be stored to indicate overflow and short-circuit conditions.

#### OPERATING FREQUENCIES AND MODULATION

The transponder of the present invention is not limited to any particular operating frequency. The choice of operating frequency will depend largely upon factors such as where the transponder is mounted, in relationship to the object it is monitoring, the location of the reader antenna (108), and relevant government regulations permitting (conversely, restricting) data transmissions of the type set forth herein in selected portions of the overall RF frequency spectrum.

An example of suitable operating frequencies for operating the transponder in the United States is 60 KHz to 490 KHz.

The transponder can be polled (and powered) by the reader/interrogator at an first "interrogation" frequency ( $F_i$ ), and the data stream can be transmitted back to the reader/interrogator at a second "data carrier" frequency ( $F_c$ ) which is, conveniently, a whole number multiple or fraction of the interrogating frequency. For example,  $F_c = F_i/2$ . Or,  $F_c = F_i/4$ . The frequency ( $F_c$ ) at which the data stream is transmitted back to the reader/interrogator is independent of the data rate, which is established by the clock generator 224 and the baud rate generator 248. However, one having ordinary skill in the art to which the present invention most

nearly pertains will recognize that the range of available  
baud rates will typically be significantly less than the  
interrogation frequency ( $F_i$ ). The baud rate is preferably  
derived from the interrogation frequency ( $F_i$ ) of the  
5 reader/interrogator, such as a whole number fraction thereof.  
For example, the baud rate may be set at  $F_i/32$  (or, in the  
case of  $F_c=F_i/2$ , the baud rate can be set to  $F_c/16$ ).

For example, the interrogation frequency ( $F_i$ ) may be 125  
KHz, and the data carrier ( $F_c$ ) may be set to 62.5 KHz, or  
10 half of the interrogation frequency.

In another example, an interrogation frequency ( $F_i$ ) of  
13.56 MHz has been found to be suitable.

The data stream, such as the exemplary data stream  
described with respect to Figure 3C is impressed by the  
15 modulator circuit 246 onto the antenna 212, and transmitted  
to the reader/interrogator. It is within the scope of this  
invention that any suitable modulation scheme be employed,  
including amplitude modulation (AM), frequency modulation  
(FM), frequency shift keying (FSK), and phase shift keying  
20 (PSK). However, phase shift keyed (PSK) is preferred. AM  
modulation is not particularly well-suited to digital  
transmission. Frequency modulation schemes such as FM or FSK  
may be somewhat problematic with regard to propagating the  
data-modulated transponder output signal through the medium  
25 of a pneumatic tire.

#### OBTAINING A TEMPERATURE-COMPENSATED PRESSURE READING

Figure 4 illustrates a relevant portion of a reader  
portion of a reader/interrogator 400. It should clearly be  
understood that the transponder of the present invention is  
30 suitable for use with virtually any suitably configured  
reader interrogator. The description that follows is limited  
to broad architectural functions that would be performed in  
the reader/interrogator. One having ordinary skill in the art  
to which the present invention most nearly pertains would be  
35 able, from the description set forth herein, to implement  
these functions in an otherwise "generic"

reader/interrogator.

The data-modulated transponder output signal is received by the antenna 410 (compare 210) of the reader/interrogator 400 (compare 200). The received signal is de-modulated and  
5 de-coded in a de-modulator/decoder circuit 420 (DE-MOD/DECODE) so that the different portions of the data stream can be properly segregated from one another. The data relating to temperature and pressure calibration (TEMP COMP, PRESS COMP, TEMP/PRESS SLOPES), the temperature count ( $N_t$ ) and  
10 the pressure count ( $N_p$ ) are provided to an arithmetic logic unit 422 capable of generating a true, temperature-compensated pressure signal ("PRESSURE") on a line 423 to the display 412 (compare 112) as well as a calibrated temperature signal ("TEMPERATURE") on the line 423. This information can  
15 be displayed to the user either selectively or simultaneously with other relevant information such as the state of the MTMS switch 220, as well as data (DATA) relating to tire identification and the like.

While the invention has been described in combination  
20 with embodiments thereof, it is evident that many alternatives, modifications, and variations will be apparent to those skilled in the art in light of the foregoing description. Accordingly, the invention is intended to embrace all such alternatives, modifications and variations  
25 as fall within the spirit and broad scope of the appended claims.

## CLAIMS

What is claimed is:

5

1. In an integrated circuit (IC) chip, a method of measuring temperature comprising:

10 flowing a current through a resistor ( $R_{ext}$ ), the resistance value of which is substantially independent of temperature, said current being a function of an absolute temperature of a transistor (Q1) resident on the IC chip, said transistor being of a type which exhibits a predictable change in its base-emitter voltage over a temperature range; and

15 mirroring the current flowing through the precision resistor to a circuit (254, 312) on the IC chip, said circuit providing an output signal ( $F_{osc}$ ) which is proportional to the current flowing through the resistor.

2. The method of claim 1, wherein:

20 the circuit is a relaxation oscillator, and the output of the circuit is a temperature-dependent frequency.

3. The method of claim 1, wherein:

25 the circuit includes at least one internal capacitor ( $C_{FX}$ ); and further comprising:

selectively switching (350) an external capacitor ( $C_p$ ) across the at least one internal capacitor to alter a characteristic of the output signal.

Figure 1  
Prior Art

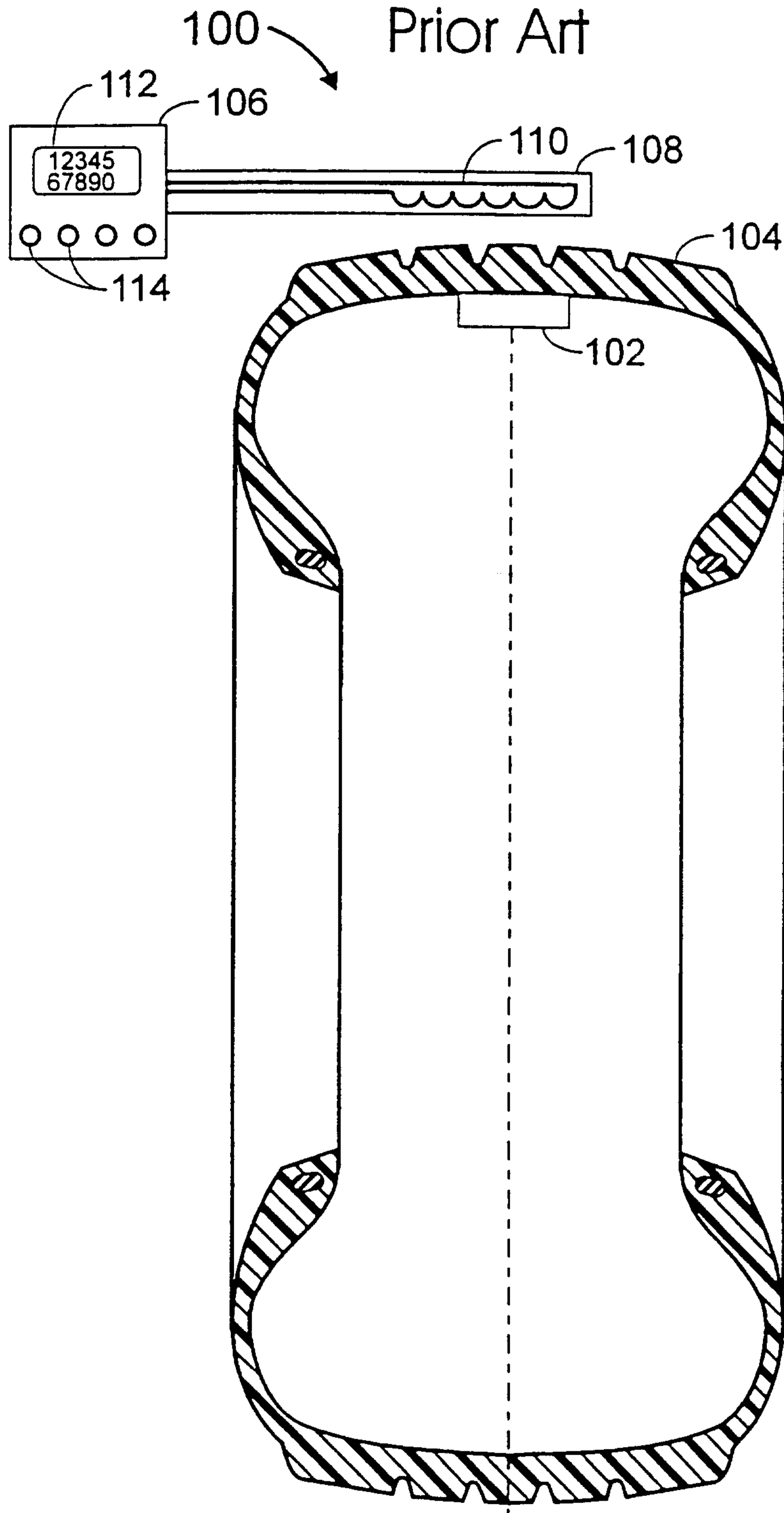
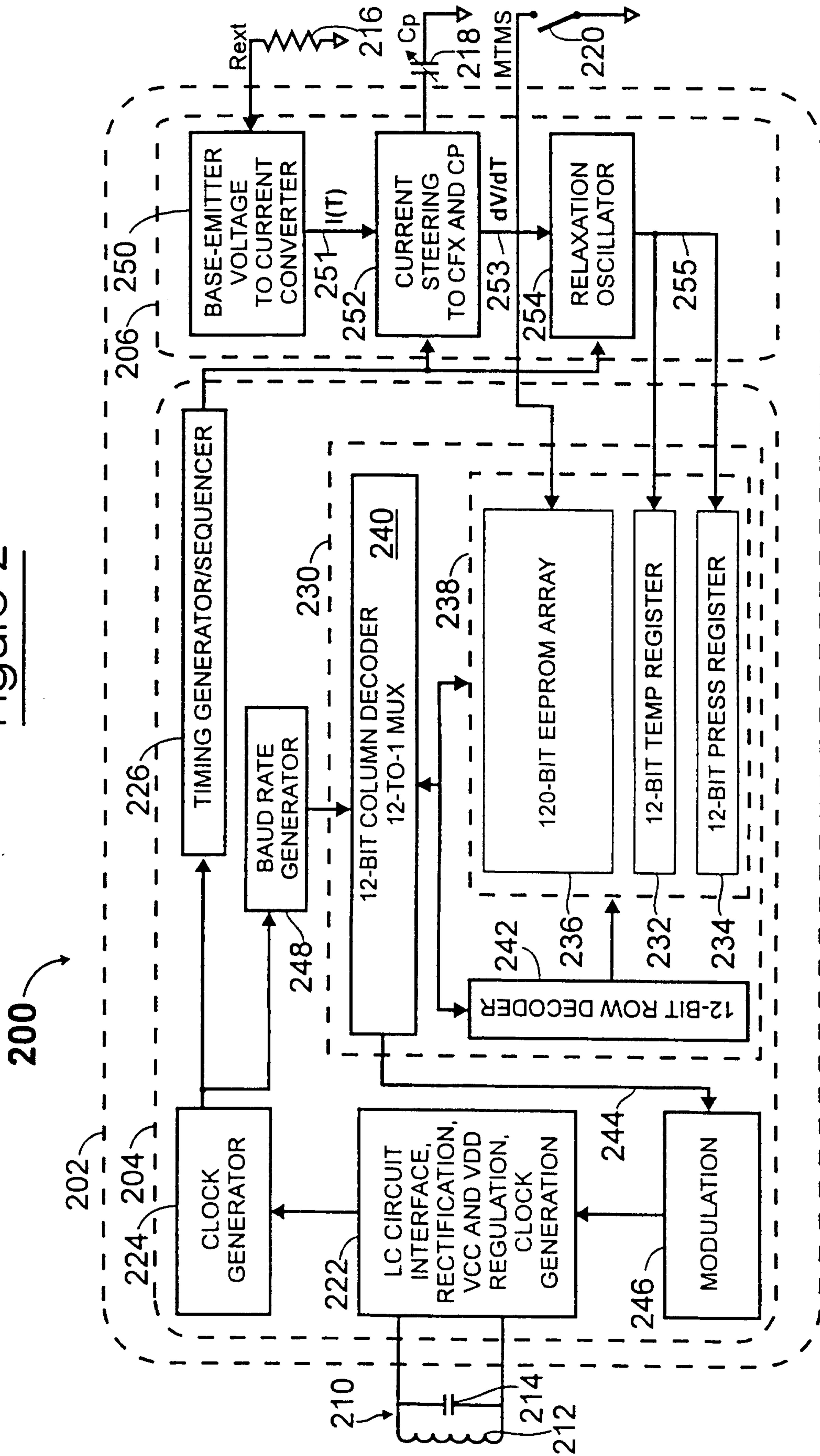


Figure 2



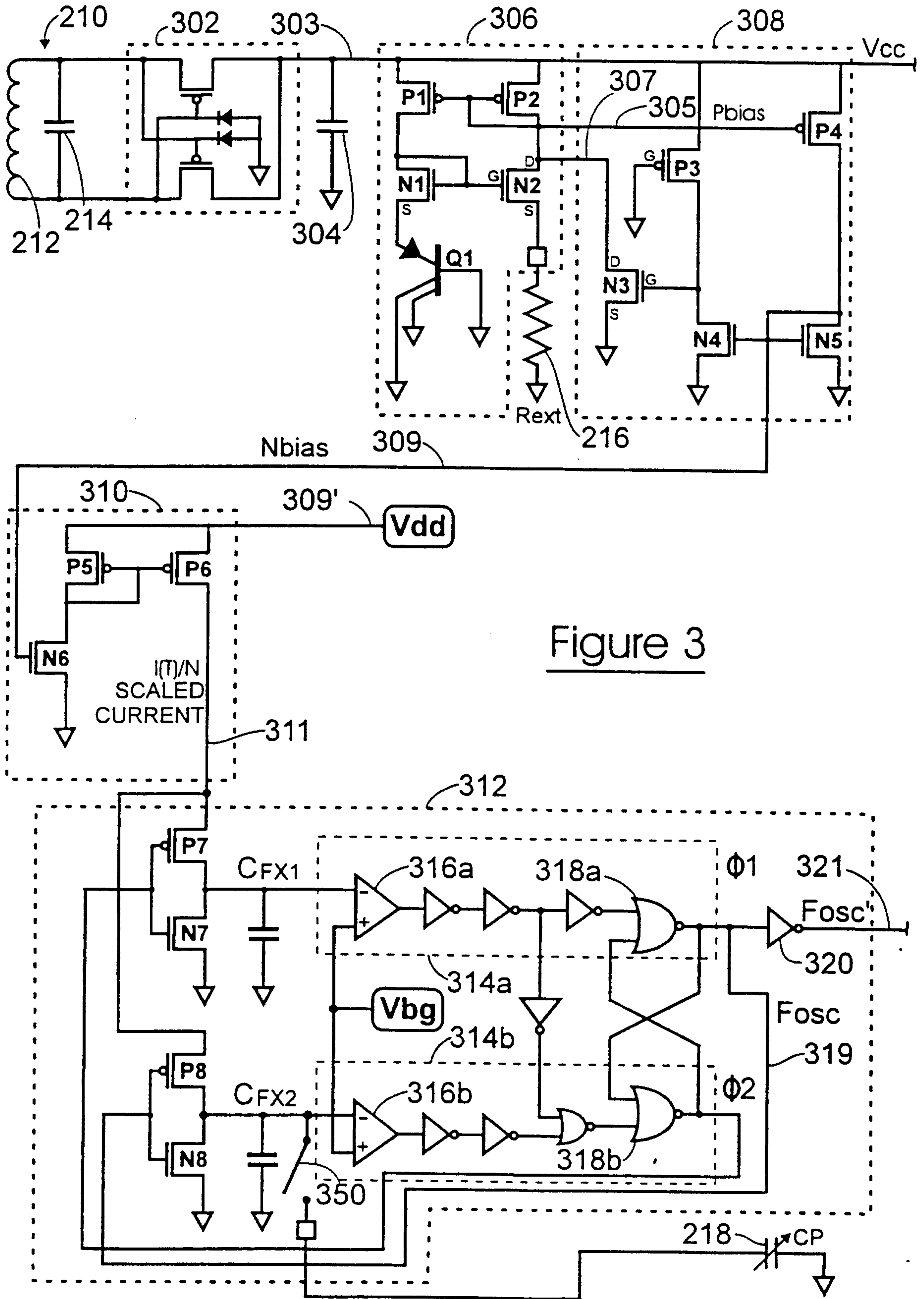
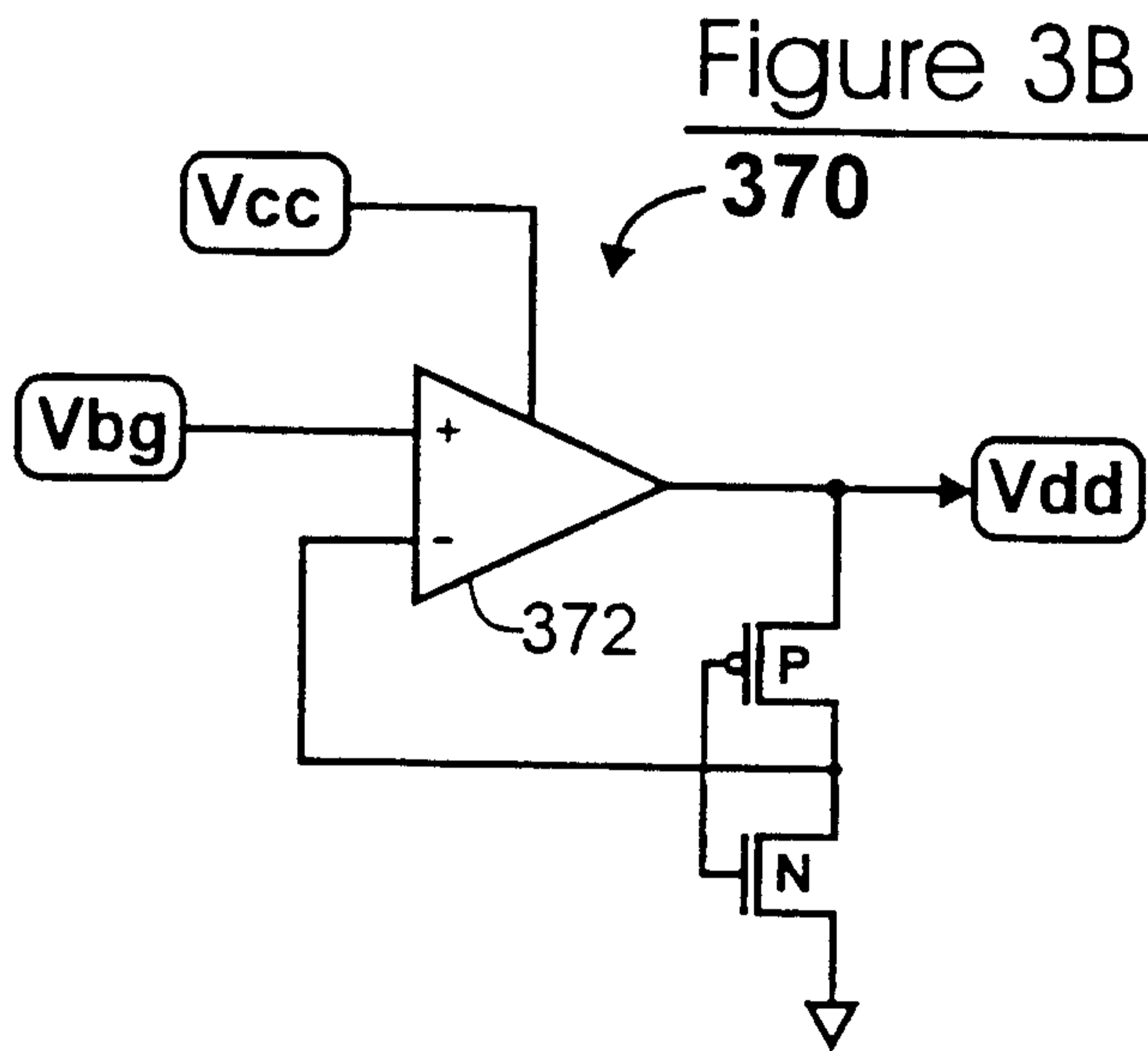
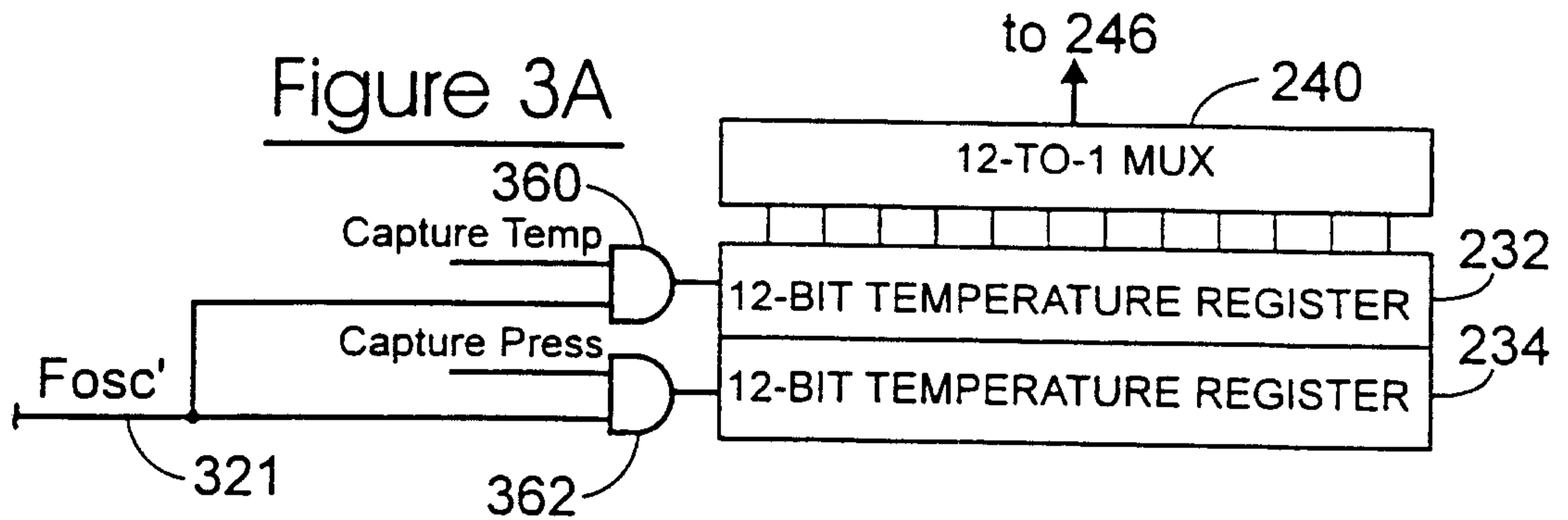


Figure 3



**Figure 3C**

← 12 COLUMNS →

ROW 1	SYNC 000..011
ROW 2	DATA 012..023
ROW 3	DATA 024..035
ROW 4	DATA 036..047
ROW 5	DATA 048..059
ROW 6	DATA 060..071
ROW 7	DATA 072..082, MTMS 083
ROW 8	TEMP COMP 084..095
ROW 9	PRESS COMP 096..107
ROW 10	TEMP/PRESS SLOPES 108..113, 114..119
ROW 11	TEMP COUNT (NT) 120..131
ROW 12	PRESS COUNT (NP) 132..143

Figure 4

