

(12) PATENT
(19) AUSTRALIAN PATENT OFFICE

(11) Application No. AU 199726721 B2
(10) Patent No. 725189

(54) Title
Method and apparatus for interference rejection with different beams,
polarizations, and phase references

(51)⁶ International Patent Classification(s)
H04B 007/08 H04B 007/10
H04B 007/02

(21) Application No: 199726721 (22) Application Date: 1997.04.14

(87) WIPO No: W097/40588

(30) Priority Data

(31) Number (32) Date (33) Country
08/634719 1996.04.19 US

(43) Publication Date : 1997.11.12
(43) Publication Journal Date : 1998.01.22
(44) Accepted Journal Date : 2000.10.05

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(56) Related Art
WO 96/04738
US 5499272

OPI DATE 12/11/97 APPLN. ID 26721/97
AOJP DATE 22/01/98 PCT NUMBER PCT/US97/06343

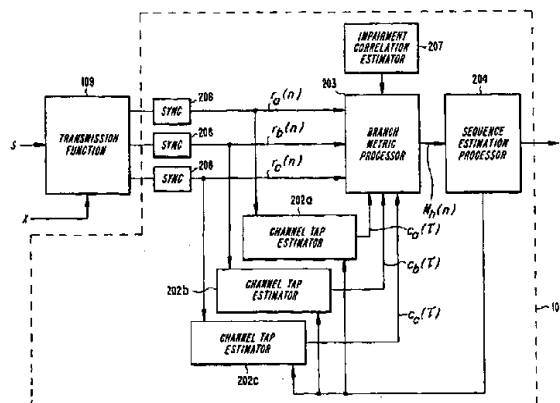


AU9726721

INTF

(51) International Patent Classification: H04B 7/08, 7/10, 7/02		A1	(11) International Publication Number: WO 97/40588
		(43) International Publication Date:	30 October 1997 (30.10.97)
(21) International Application Number: PCT/US97/06343		(81) Designated States: AL, AM, AT, AU, AZ, BA, BB, BG, BR, BY, CA, CH, CN, CU, CZ, DE, DK, EE, ES, FI, GB, GE, HU, IL, IS, JP, KE, KG, KP, KR, KZ, LC, LK, LR, LS, LT, LU, LV, MD, MG, MK, MN, MW, MX, NO, NZ, PL, PT, RO, RU, SD, SE, SG, SI, SK, TJ, TM, TR, TT, UA, UG, UZ, VN, ARIPO patent (GH, KE, LS, MW, SD, SZ, UG), Eurasian patent (AM, AZ, BY, KG, KZ, MD, RU, TJ, TM), European patent (AT, BE, CH, DE, DK, ES, FI, FR, GB, GR, IE, IT, LU, MC, NL, PT, SE), OAPI patent (BF, BJ, CF, CG, CI, CM, GA, GN, ML, MR, NE, SN, TD, TG).	
(22) International Filing Date: 14 April 1997 (14.04.97)		Published With international search report.	
(30) Priority Data: 08/634,719 19 April 1996 (19.04.96) US			
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(54) Title: METHOD AND APPARATUS FOR INTERFERENCE REJECTION WITH DIFFERENT BEAMS, POLARIZATIONS, AND PHASE REFERENCES



(57) Abstract

A digital radio communication system includes processing to jointly mitigate the deleterious effects of fading, time dispersion and interference using interference rejection and diversity combining. The system employs a selection processor for preliminarily reducing the number of signals for interference rejection and diversity combining based on one or more criterion. The system accommodates signals from dual polarized antennas. In one particular embodiment, the system performs interference rejection and diversity combining by separating a received signal into its in-phase and quadrature components.

**METHOD AND APPARATUS FOR INTERFERENCE REJECTION WITH
DIFFERENT BEAMS, POLARIZATIONS, AND PHASE REFERENCES**

5

BACKGROUND

The present invention pertains to processing of radio communication signals to offset the effects of multipath fading, time dispersion and channel interference. The invention more specifically pertains to performing the above identified signal processing using signals derived from a variety of different antenna designs, or using signals separated into in-phase and quadrature components.

In a practical radio communication system, there commonly co-exists a number of phenomena which degrade the quality of transmitted signals. Among the most troublesome phenomena are flat fading, time dispersion, and channel interference.

Flat fading and time dispersion are multipath effects caused by the interference of a main transmitted signal and its reflections or echos (which may be caused by the surrounding terrain). When the path lengths are relatively small, the multiple signals will arrive at the receiver at almost the same time. The signals add either constructively or destructively, giving rise to flat fading having a Rayleigh distribution. When the path lengths are relatively large, the transmission medium is considered time dispersive, and the added signals can be viewed as echoes of the transmitted signal. The echoes are delayed with respect to the main ray. Time dispersion gives rise to intersymbol interference (ISI).

Channel interference arises due to the presence of sources which are not orthogonal to the desired signal. Non-orthogonal signals, or interference, often come from radios operating on the same frequency (i.e. co-channel interference) or from radios operating on neighboring frequency bands (i.e. adjacent-channel interference). Non-orthogonal signal sources are referred to as interferers.

Fading can be mitigated by having multiple receive antennas and employing some form of diversity combining, such as selective combining, equal gain combining, or maximal ratio combining. Diversity takes advantage of the fact that the fading on the different antennas is not the same, so that when one antenna has a faded

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signal, chances are the other antenna does not. Note Mobile Communications Design Fundamentals by William C. Y. Lee, Howard W. Sams & Co., Indiana, USA. In section 3.5.1 of this book, several examples are given describing how signals from two receiver amplifiers with separate antennas can be combined to counteract fading.

5 Time dispersion may be advantageously corrected by using an equalizer. In the case of digital signal modulation, a maximum likelihood sequence estimation (MLSE) equalizer such as described in Digital Communications, 2nd Ed., by John G. Proakis, Mc-Graw Hill Book Company, New York, New York, USA, 1989 may be used. In section 6.7 of this book, various methods are described for detecting signals
10 corrupted by time dispersion, or inter-symbol interference (ISI), using MLSE equalization.

 The impact of channel interference may be reduced by employing array processing techniques with multiple antennas. For example, adaptive beamforming can be used to "steer" a null in the antenna pattern in the direction of an interferer.

15 More recently, methods have been proposed that partially solve the problems of multipath fading and interference. In U.S. Patent 5,191,598 to Bäckström, et al., for example, the problem of accurately detecting signals in the presence of flat fading and time dispersion is overcome by using a Viterbi-algorithm having a transmission function estimated for each antenna. By reference thereto, U.S. Patent 5,191,598 is
20 incorporated herein in its entirety. Another method of accurately detecting signals in the presence of flat fading and interference was presented in the IEEE Transactions on Vehicular Technology, Vol. 42, No. 4, Nov. 1993, J. H. Winters: "Signal Acquisition and Tracking with Adaptive Arrays in the Digital Mobile Radio System IS-54 with Flat Fading".

25 Although the above described techniques greatly improve signal quality, there remains room for improvement. Including separate processing modules to separately address fading, time dispersion and interference adds to the cost and complexity to the device.

 Furthermore, algorithms (such as Viterbi's) can not cost-effectively handle a
30 large number of diversity branches. It would be desirable to provide some way of culling out a smaller number of diversity branches prior to performing interference

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rejection and diversity combining to reduce the computational complexity and hardware requirements of the receiver.

Finally, the above-described techniques fail to provide a receiver design which could be easily adapted to a variety of antenna configurations, such as phased array
5 antennas or antennas producing signals having different polarizations. It would be desirable to provide a technique for reducing the deleterious effects of signal transmission which would accommodate a wide variety of antenna configurations. There is further need to reduce deleterious effects of signal transmission in the situation where the in-phase and quadrature components of the interference are
10 correlated.

SUMMARY

Accordingly, it is one exemplary object of the invention to perform interference rejection combining to jointly offset the effects of flat fading, time
15 dispersion and channel interference.

It is a further exemplary object of the present invention to perform interference rejection combining in a manner which accommodates different antenna designs, such as antennas producing signals having different polarizations.

It is a further exemplary object of the present invention to perform interference
20 rejection combining for radiocommunication signals separated into in-phase and quadrature components.

The present invention achieves the above objectives, as well as additional objectives, according to exemplary embodiments of the present invention, by employing a method and apparatus for generating and transmitting a signal
25 representing a transmitted symbol sequence and receiving the signal on at least two separate antennas. The signal is processed to produce received signal samples for each of the antennas. Channel taps are estimated for each of the antennas. Impairment correlation properties between antennas are also estimated. Branch metrics are formed in a branch metric processor using the received signal samples and
30 the channel tap and impairment correlation estimates. The branch metrics are

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employed in a sequence estimation algorithm to estimate the transmitted symbol sequence.

In one exemplary embodiment, branch metrics are formed by generating hypothetical symbol sequences and filtering the hypothetical signal sequences with the
5 channel tap estimates to produce hypothesized received signal samples for each antenna. The hypothesized received signal samples are subtracted from the received signal samples to produce hypothesized error signals which are processed with the estimate of impairment correlation properties to produce branch metrics.

In another exemplary embodiment, an estimate of impairment correlation
10 properties is formed by generating tentative detected symbol sequences which are filtered with the channel tap estimates to produce detected signal samples for each antenna. The detected signal samples are subtracted from the received signal samples to produce detected error signals which are processed with the estimate of impairment correlation properties to produce an update of the estimate of the impairment
15 correlation properties.

According to another particularly beneficial embodiment of the present invention, the above described method and apparatus can be used in conjunction with a variety of different antenna designs and configurations. This embodiment employs a selection processor which selects N output signals from M input signals received from
20 an antenna or beamforming processor (where $M \geq N$). The selection processor chooses the N signals (out of M) that meet one or more criteria. For instance, the selection processor may choose a set of N signals having acceptable instantaneous branch power, acceptable average branch power, acceptable beam center direction relative to desired signal direction, and/or acceptable signal quality as gauged from a
25 sync word.

According to one exemplary embodiment, the selection processor interfaces with M co-phased antenna elements which may be a combination of both horizontally and vertically polarized antenna elements. The signals received by the M co-phased antenna elements are fed to a fixed beamforming processing, and thereafter sent to the
30 selection processor. Alternatively, the signals from the M co-phased antenna elements are fed to two fixed beamforming processors. One of the two fixed beamforming

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processors processes the vertically polarized signals, while the other processes the horizontally polarized signals. Instead of vertical and horizontal polarization, other types of orthogonal polarization may be used.

According to another exemplary embodiment, the selection processor interfaces
5 with sector antennas, where the antennas may be either vertically or horizontally polarized. In this embodiment, antennas with the same polarization can be physically separated. Again, instead of vertical and horizontal polarization, other types of orthogonal polarization may be used.

In yet another particularly beneficial embodiment of the present invention, the
10 input radio signal is separated into its in-phase and quadrature components. The in-phase and quadrature components are processed as if they were received from separate antenna elements.

According to this embodiment, the invention includes a method and apparatus
for receiving a radio signal on at least one antenna element representing a transmitted
15 symbol sequence. This radio signal is processed to produce received signal samples for the at least one antenna. A channel tap is estimated for the at least one antenna, as are scalar correlation properties. A branch metric is formed using a scalar branch metric processor on the basis of the received signal samples, the channel tap estimate, and the scalar estimate of impairment correlation properties. The scalar branch metric
20 is, in turn, used in a sequence estimation algorithm to estimate the transmitted symbol sequence.

According to another embodiment of the invention, branch matrices are formed
by generating hypothetical symbol sequences. These hypothetical signal sequences are filtered with the channel tap estimate to produce hypothesized received signal samples
25 for the at least one antenna. The hypothesized received signal samples are subtracted from the received signal samples to produce complex error signals. These complex error signals are processed with the scalar estimate of impairment correlation properties to produce branch metrics. More particularly, this last step involves extracting an in-phase phase component from the complex error signal, and extracting
30 a quadrature component of the complex error signal, and performing processing on the in-phase component and the quadrature component to produce the branch metrics.

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According to another embodiment of the invention, the impairment correlation properties are estimating by first generating tentative detected symbol sequences. These tentative detected symbol sequences are filtered with the scalar channel tap estimate to produce estimated received signal samples for the at least one antenna.

5 The estimated received signal samples are subtracting from the received signal samples to produce impairment signal samples. These impairment signal samples are processed with the estimate of scalar impairment correlation properties to produce an updated estimate of said scalar impairment correlation properties. More specifically, this last step includes extracting an in-phase phase component from the impairment

10 signal samples, and extracting a quadrature component of the impairment signal samples, and performing processing on these components.

According to still another exemplary embodiment of the present invention, a plurality of branch metric processors are employed, each of which processes a different group of signals. More specifically, this embodiment entails

15 receiving a number of M radio signals representing a transmitted symbol sequence and selecting therefrom groups of radio signals using a selection processor. The groups of radio signals are processed to produce branch metrics. These branch metrics are added together to produce combined branch metrics. The combined branch metrics is then employed in conjunction with a sequence estimation algorithm to estimate the

20 transmitted symbol sequence.

BRIEF DESCRIPTION OF THE DRAWINGS

These and other features and advantages of the present invention will be readily apparent to one skilled in the art from the following written description when

25 read in conjunction with the drawings in which like reference numerals refer to like elements.

Figure 1 is an exemplary illustration of a digital radio communication system;

Figure 2 is an exemplary illustration of a receiver processor and transmission function according to the present invention using a vector branch metric processor;

30 Figure 3 is an exemplary illustration of a transmission function;

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Figure 4 is an exemplary illustration of a vector metric processor according to the present invention;

Figure 5 is an exemplary illustration of a vector adaptive estimator of the impairment correlation properties;

5 Figure 6 is an exemplary illustration of an embodiment consisting of vertical and horizontal antenna elements with a single fixed beamforming processor;

Figure 7 is an exemplary illustration of an embodiment consisting of vertical and horizontal antenna elements with separate fixed beamforming processors for the vertical and horizontal elements;

10 Figure 8 is an exemplary illustration of an embodiment consisting of vertical and horizontal antennas with no fixed beamforming processor;

Figure 9 is an exemplary illustration of an embodiment of the branch selection processor that chooses N antenna signals from M ($N \leq M$) possible signals based upon some signal quality measure.

15 Figure 10 is an exemplary illustration of a receiver processor and transmission function according to the present invention using a scalar branch metric processor;

Figure 11 is an exemplary illustration a scalar branch metric processor according to the present invention; and

20 Figure 12 is an exemplary illustration of a scalar correlation estimator according to the present invention.

Figure 13 is an exemplary illustration of an embodiment employing a plurality of branch metric processors.

DETAILED DESCRIPTION

25 In the following description, for purposes of explanation and not limitation, specific details are set forth, such as particular circuits, circuit components, techniques, etc. in order to provide a thorough understanding of the invention. However it will be apparent to one skilled in the art that the present invention may be practiced in other embodiments that depart from these specific details. In other instances, detailed descriptions of well-known methods, devices, and circuits are
30 omitted so as not to obscure the description of the present invention with unnecessary detail.

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A. Description of Embodiment having Two Antennas and a Branch Metric Processor

A radio transmitter and receiver system for a radio communication system is illustrated schematically in Figure 1. The radio communication system may operate using frequency division multiple access (FDMA), time division multiple access (TDMA), or code division multiple access (CDMA), or some combination thereof. A transmitter has a digital symbol generator **102** which receives an information carrying signal **101** and generates a corresponding digital symbol sequence, S . The symbol sequence S is subjected to digital to analog (D/A) conversion, modulation, pulse shape filtering, amplification, and is transmitted as analog signal Y by digital transmitter **103** according to known techniques.

In addition to thermal noise, there may also exist an interferer **108** transmitting signal X which may be non-orthogonal to signal Y . Signals Y and X travel through separate radio channels and are intercepted by antennas **104** which are D in number.

Radio units **105** amplify, downconvert, and filter the received signals according to known methods to produce analog signals. Each analog signal is coupled to an analog-to-digital (A/D) converter **106**, which converts the analog signal into a received signal sample stream $r_d(kT_s)$, where T_s is the sample period, the reference numeral k is an integer counter, and the subscript d indicates that the signal arrives from the d^{th} antenna $1 \leq d \leq D$. The sampling period T_s may be less than the symbol period T . The received signal sample streams are collected in processor **107**, which processes these streams to produce an estimate of the transmitted digital symbol stream, $\hat{S}$. In later descriptions, transmission function **109** is used to refer to the signal path through digital transmitter **103**, the radio transmission channel (not shown in Figure 1), antennas **104**, radio units **105** and A/Ds **106** collectively.

The processing unit **107** is illustrated in greater detail in Figure 2 where, for simplicity, the number D of antennas is restricted to three: designated a , b , and c . Processing unit **107** may be, for example, a Digital Signal Processor (DSP) such as a TMS320C50 manufactured by Texas Instruments. The function of processing unit **107** is to produce an estimate of the transmitted digital symbol stream $\hat{S}$ which accurately corresponds to the symbol sequence S which was originally transmitted.

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Transmission function **109** produces the received signal sample streams $r_a(kT_s)$, $r_b(kT_s)$, and $r_c(kT_s)$ which are sent to processing unit **107** where they are processed in accordance with the present invention. The received signal sample streams $r_a(kT_s)$, $r_b(kT_s)$, and $r_c(kT_s)$ are coupled to a signal pre-processor, or sync, block **206** where

5 the received signal sample streams are correlated with known timing/synchronization sequences as described, for example, by Giovanna, et al. "Fast Adaptive Equalizers for Narrow-Band TDMA Mobile Radio", IEEE Transactions on Vehicular Technology, Vol. 40, No. 2, May 1991, pp. 392-404. For the case of symbol-spaced demodulation, if the sample period T_s is less than symbol period, T , the signal pre-

10 processor **206** performs a decimation of the received signal sample streams $r_a(kT_s)$, $r_b(kT_s)$, and $r_c(kT_s)$ to produce one sample per symbol: designated $r_a(n)$, $r_b(n)$, and $r_c(n)$ respectively. For the case of fractionally-spaced demodulation, more than one sample per symbol is generated.

Estimating circuits **202a**, **202c**, and **202c** produce channel tap estimates $c_a(\tau)$, $c_b(\tau)$, and $c_c(\tau)$ which are used to model the radio transmission channel associated with each particular antenna. Initial channel tap estimates can be obtained from sync correlation values or least-squares estimation according to known techniques. If the channel must be tracked, it is typical to use received data and tentative symbol estimate values generated in the sequence estimation processor **204**. Channel tracking

15 is known to those skilled in the art as discussed, for example, in Digital Communications 2nd Ed. by Proakis as previously mentioned, and by A. P. Clark and S. Hariharan, "Adaptive Channel Estimates for an HF Radio Link", IEEE Trans. on Communications, vol. 37, pp. 918-926, Sept. 1989. The channel tap estimates $c_a(\tau)$, $c_b(\tau)$, and $c_c(\tau)$ are coupled to the input of the branch metric processor **203**.

25 Also coupled to the branch metric processor **203** is an estimate of the impairment correlation properties obtained from impairment correlation estimator **207**. The estimate of the impairment correlation properties comprises information regarding the impairment correlation properties between the receive antennas **104**. The impairment correlation estimator uses impairment process estimates to update and

30 possibly track the estimate of the impairment correlation properties which is discussed in further detail in the ensuing text and figures.

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Branch metric processor **203** uses received signal samples $r_a(n)$, $r_b(n)$, and $r_c(n)$, channel tap estimates $c_a(\tau)$, $c_b(\tau)$, and $c_c(\tau)$, and the estimate of the impairment correlation properties to form branch metric $M_b(n)$. This branch metric is used, for example, in a sequence estimation processor **204** to develop tentative and final estimates of the transmitted symbols.

The transmission function **109** is illustrated in greater detail in Figure 3 where, for simplicity, the number of interferers is restricted to one. It will be apparent to one skilled in the art that the present invention may also be used for the case where there are two or more interferers. The transmit function **109** begins with the signal path for the symbol sequence S through digital transmitter **103** which transmits analog signal Y . The analog signal Y propagates through a separate radio transmission channel to each of the three receiver antennas: radio channel **301a** to receiver antenna **104a**, radio channel **301b** to receiver antenna **104b**, and radio channel **301c** to receiver antenna **104c**. Similarly, interference signal X also propagates through three other separate radio channels **302a-302c** to receiver antennas **104a-104c** respectively. Radio channels **301a-301c** and **302a-302c** may introduce fading and time dispersion. Omnipresent thermal noise processes $n_a - n_c$ are also received by receiver antennas **104a-104c** respectively. Each antenna **104a-104c** is coupled to a radio unit **105a-105c** respectively which amplifies, downconverts, and filters the received signals according to known methods to produce an analog signal. Each analog signal is coupled to an analog-to-digital (A/D) converter **106a-106c** which converts the analog signals into received signal sample streams $r_a(kT_s)$, $r_b(kT_s)$, and $r_c(kT_s)$. One method for conversion from analog to digital is to use log-polar signal processing, as described in U. S. Patent 5,048,059 to Dent, the disclosure of which is incorporated by reference herein in its entirety. For subsequent processing, a conversion from log-polar to rectangular samples is made, so that, for example, I and Q samples, sometimes referred to as complex samples, are used. By using log-polar signal processing initially, a limiting receiver which provides signal strength and phase samples can be used, and adaptive gain control can be made simple.

In an MLSE equalizer, different possible transmitted symbol sequences S are considered. In one implementation, hypothesized symbol values $s_b(n)$ are filtered by

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- channel tap estimates $c_a(\tau)$, $c_b(\tau)$, and $c_c(\tau)$ to produce hypothesized received samples $r_{a,h}(n)$, $r_{b,h}(n)$, and $r_{c,h}(n)$ for each antenna. The differences between the hypothesized $r_{a,h}(n)-r_{c,h}(n)$ and the actual $r_a(n)-r_c(n)$ received signal sample streams, referred to as the hypothesis errors, give an indication of how good a particular hypothesis is. The squared magnitude of the hypothesis error is used as a metric to evaluate a particular hypothesis. The metric is accumulated for different hypotheses for use in determining which hypotheses are better using the sequence estimation algorithm. This process may be efficiently realized using the Viterbi algorithm, which is a known form of dynamic programming. A description of the Viterbi algorithm may be found in
- 10 Forney, G., "The Viterbi Algorithm", Proc. of the IEEE, vol. 61, pp. 268-278, March, 1973. As will be apparent to one skilled in the art, other sequence estimation algorithms, such as the M-algorithm, may also be used.

- In an MLSE equalizer, there are states associated with different symbol sequence hypotheses $s_h(n)$. At a given iteration, there are previous states: each
- 15 associated with an accumulated metric. Each pairing of a previous state with a current state results in a branch metric, $M_h(n)$. The candidate metric for a current state is then the sum of the branch metric $M_h(n)$ and the previously accumulated metric. For each current state, the previous state which gives the smallest candidate metric is selected as the predecessor state, and the smallest candidate metric becomes
- 20 the accumulated metric for the current state. For metric combining, as described in aforementioned U.S. Patent 5,191,598, the branch metric can be expressed as:

$$M_h(n) = [\mathbf{r}(n) - \mathbf{C}\mathbf{s}_h(n)]^H \mathbf{D} [\mathbf{r}(n) - \mathbf{C}\mathbf{s}_h(n)]$$

where:

$$\mathbf{r}(n) = [r_a(n) \ r_b(n) \ r_c(n)]$$

$$\mathbf{C} = \begin{bmatrix} c_a(0) & \dots & c_a(N_t-1) \\ c_b(0) & \dots & c_b(N_t-1) \\ c_c(0) & \dots & c_c(N_t-1) \end{bmatrix}$$

$$\mathbf{s}_h(n) = [s_h(n) \ s_h(n-1) \ \dots]^T$$

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$$D = \begin{bmatrix} K_a & 0 & 0 \\ 0 & K_b & 0 \\ 0 & 0 & K_c \end{bmatrix}$$

The channel tap estimates for each signal received on antenna 104a-104c are designated by $c_a(\tau)$, $c_b(\tau)$, $c_c(\tau)$ respectively where τ is the delay (i.e. $\tau = 0$ is the main ray, $\tau = 1$ is the first echo, etc.). N_t is the number of channel taps estimated per antenna and K_a , K_b , K_c are weighting coefficients for antennas 104a-104c respectively.

The present invention takes advantage of the fact that, from a diversity and equalization point-of-view, the impairment (interference + noise) on multiple receive antennas 104 is often correlated at any specific moment in time, even though, on the average, it may be uncorrelated. By expanding diversity combining techniques to exploit this correlation, significant gains are realized. For optimal performance, a whitening, or decorrelation, process may be applied and the optimum branch metric may include the inverse of the impairment correlation matrix. The optimum branch metric $M_b(n)$ according to the present invention is:

$$M_b(n) = [\mathbf{r}(n) - \mathbf{C}(n) \mathbf{s}_b(n)]^H \mathbf{A}(n) [\mathbf{r}(n) - \mathbf{C}(n) \mathbf{s}_b(n)] = \mathbf{e}_b^H(n) \mathbf{A}(n) \mathbf{e}_b(n)$$

where:

$$\mathbf{A}(n) = \mathbf{R}_{zz}(n)^{-1}, \text{ or a related quantity; } \mathbf{R}_{zz}(n) = \mathbf{E}(\mathbf{z}(n) \mathbf{z}^H(n))$$

$$\mathbf{z}(n) = [z_a(n) \ z_b(n) \ z_c(n)]^T; \quad \mathbf{e}_b(n) = \mathbf{r}(n) - \mathbf{C}(n) \mathbf{s}_b(n)$$

The time varying nature of the channel and the impairment correlation are denoted with time index n . The $\mathbf{R}_{zz}(n)$ matrix is referred to as the impairment correlation matrix at discrete time, n . The $\mathbf{A}(n)$ matrix (i.e., the A-matrix) is the inverse of the $\mathbf{R}_{zz}(n)$ matrix, or a related quantity such as the adjoint or pseudo-inverse. As will be apparent to those skilled in the art, $\mathbf{R}_{zz}(n)$ and $\mathbf{A}(n)$ are specific examples of

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impairment correlation properties of which other forms are known. Throughout the following, the term A-matrix is used generically to refer to any estimate of the impairment correlation properties.

The impairments on antennas **104a-104c** at time n are designated by $z_a(n)$, $z_b(n)$, and $z_c(n)$ respectively. For a given hypothesis, $e_h(n)$ is an estimate of the impairment process. As shown above, the A-matrix, $A(n)$, is the inverse of the impairment correlation matrix $R_{zz}(n)$. For the case of uncorrelated impairment (*i.e.*, no interferer) the A-matrix reduces to diagonal matrix D . When the signal is known or detected correctly, the impairment is given by:

$$\mathbf{z}(n) = \mathbf{r}(n) - \mathbf{C}(n) \mathbf{s}_{\text{det}}(n)$$

10 where:

$$\mathbf{s}_{\text{det}}(n) = [s_{\text{det}}(n) s_{\text{det}}(n-1) \dots]^T$$

Note that $s_{\text{det}}(n)$ is the known or detected symbol sequence at time n .

Determination of the A-matrix for use in the present invention can be performed in a number of ways depending upon the specific application and the required performance. The simplest approach is to use a fixed set of values for the A-matrix, stored in memory. These values depend primarily on the configuration of the receive antennas and on the carrier frequencies being employed. An alternative approach is to determine the A-matrix from synchronization information and to keep the A-matrix values constant between synchronization, or other, known fields. At each new occurrence of the synchronization field, the A-matrix can be recomputed, with or without use of the previous A-matrix values. Another alternative approach is to use synchronization fields to initialize, or improve, the A-matrix values and then to use decisions made on the data field symbols to track the A-matrix values.

Also, consideration is given for the method used to track the A-matrix values. Since the A-matrix comprises information regarding the impairment correlation properties between the antennas **104a**, **104b**, and **104c**, standard estimation methods for estimating correlation or inverse correlation matrices can be applied. Using either known or detected symbol values, impairment values can be obtained by taking the

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differences between the received signal sample streams $r_a(n)-r_c(n)$ and the hypothesized received signal sample streams $r_{a,h}(n)-r_{c,h}(n)$. At time n , this gives a vector of impairment values, denoted $\mathbf{z}(n)$; one value for each antenna. Here, elements in the vector correspond to different antennas **104**. A straightforward way of forming the A-matrix is given by:

$$\mathbf{R}(n) = \lambda \mathbf{R}(n-1) + K \mathbf{z}(n) \mathbf{z}^H(n)$$

$$\mathbf{A}(n) = \mathbf{R}^{-1}(n)$$

K is a scaling constant, typically 1 or $\sqrt{(1-\lambda)}$. Because $\mathbf{R}(n)$ is a Hermitian matrix, only a portion of the matrix elements need be computed.

Such a straightforward approach is fairly high in complexity. One way to reduce complexity is to apply the matrix inversion lemma and update the A-matrix directly as:

$$\mathbf{A}(n) = \frac{1}{\lambda} \left[\mathbf{A}(n-1) - \left(\frac{1}{\lambda + \mathbf{z}(n)^H \mathbf{p}(n)} \right) \mathbf{p}(n) \mathbf{p}^H(n) \right]$$

where:

$$\mathbf{p}(n) = \mathbf{A}(n-1) \mathbf{z}(n)$$

Because the A-matrix is Hermitian, it is only necessary to compute those elements on the diagonal and either those elements above or below the diagonal.

These techniques for estimating and tracking the A-matrix are given only for purposes of illustration. In general, the A-matrix can be expressed and estimated in a variety of ways, as will be apparent to those skilled in the art. See, for example, the book by S. Haykin, Adaptive Filter Theory, Second Edition, Prentice-Hall, Englewood Cliffs, N.J., 1991. The present invention may also be applied to the blind equalization problem in which known synchronization sequences are absent. In this case, the A-matrix is estimated in a manner similar to how the channel is estimated.

In a first embodiment, a processor **107** having a symbol-spaced (i.e., T-spaced) equalizer is presented where the channel must be tracked over the data field,

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- or burst. This embodiment is applicable to the digital cellular system defined by the IS-136 specification which has relatively long TDMA data bursts (6.67 milliseconds) with respect to time. For this embodiment, the branch metric processor 203 is illustrated in greater detail in Figure 4 where, for simplicity, the number of antennas is further restricted to two: designated a and b. This particular embodiment has usefulness in that the use of two receive antennas is common in many cellular systems which already employ some form of diversity combining. As before, it will be apparent to those skilled in the art that this embodiment may also be employed in the case where there are three or more antennas.
- 10 The impairment correlation matrix R_{zz} and the inverse impairment correlation matrix A are defined as follows:

$$R_{zz} = P = \begin{bmatrix} p_{aa} & p_{ab} \\ p_{ab}^* & p_{bb} \end{bmatrix}$$

$$R_{zz}^{-1} = \frac{1}{(p_{aa}p_{bb} - |p_{ab}|^2)} \begin{bmatrix} p_{bb} & -p_{ab} \\ -p_{ab}^* & p_{aa} \end{bmatrix} = w \begin{bmatrix} p_{bb} & -p_{ab} \\ -p_{ab}^* & p_{aa} \end{bmatrix} = A$$

- The variable p_{aa} denotes the impairment power received on antenna a; the variable p_{bb} denotes the impairment power received on antenna b. The off-diagonal matrix elements are the cross correlation values: p_{ab} denotes the correlation of the impairment received on antenna a with the conjugate of that received on antenna b.
- 15

The branch metric then becomes:

$$M_h(n) = e_h(n)^H A(n) e_h(n) = w [p_{bb} |e_{a,h}(n)|^2 - 2 \operatorname{Re} \{ p_{ab} e_{a,h}(n) e_{b,h}^*(n) \} + p_{aa} |e_{b,h}(n)|^2]$$

where:

$$w = \frac{1}{p_{aa}p_{bb} - |p_{ab}|^2} \quad \text{and} \quad e_{d,h}(n) = r_d(n) - r_{d,h}(n)$$

The calculation of this branch metric is schematically illustrated in Figure 4.

- A symbol sequence generator 410 generates hypothesized symbol sequences $s_h(n)$. These sequences are filtered in filters 400 using channel tap estimates $c_a(\tau)$ and $c_b(\tau)$ for antennas a and b to produce hypothesized received signal samples $r_{a,h}(n)$ and
- 20

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$r_{b,h}(n)$, respectively. The hypothesized received signal samples, $r_{a,h}(n)$, are subtracted from the actual received signal samples from antenna a, $r_a(n)$, in summing junction 401 to produce error signal $e_{a,h}(n)$. Similarly hypothesized received signal samples, $r_{b,h}(n)$, are subtracted from the actual received signal samples from antenna b, $r_b(n)$, in summing junction 402 to produce error signal $e_{b,h}(n)$. Blocks 403 form the squared magnitudes of the error signals $e_{a,h}(n)$ and $e_{b,h}(n)$. The squared magnitude for error signal $e_{a,h}(n)$ is multiplied at junction 406 by multiplier m_{aa} , the result being coupled to summing junction 408. The squared magnitude for error signal $e_{b,h}(n)$ is multiplied at junction 407 by multiplier m_{bb} , the result being coupled to summing junction 408. Finally, multiplier 404 forms the product of $e_{a,h}(n)$ and $e_{b,h}^*(n)$, the product of which is subsequently multiplied by multiplier m_{ab} in multiplier 405, forming the real part only. The result is subtracted in summing junction 408, the output of which is the branch metric $M_h(n)$. The multipliers m_{aa} , m_{bb} , and m_{ab} are related to the impairment correlation matrix by:

$$\begin{aligned} m_{aa} &= w p_{bb} \\ m_{bb} &= w p_{aa} \\ m_{ab} &= 2w p_{ab} \end{aligned}$$

As will be apparent to those skilled in the art the w term is common to the branch metric calculation and may be applied in a different manner or even omitted when the denominator to w approaches zero.

At time n , the A matrix elements are updated as:

$$\begin{aligned} p_{aa}(n+1) &= \lambda p_{aa}(n) + |e_a(n)|^2 K \\ p_{ab}(n+1) &= \lambda p_{ab}(n) + e_a(n) e_b^*(n) K \\ p_{bb}(n+1) &= \lambda p_{bb}(n) + |e_b(n)|^2 K \end{aligned}$$

K is a scaling factor which, if equal to unity, is dropped from the calculation to reduce the number of computations. K may be derived from λ which is the so-called "forgetting factor".

A schematic illustration of the impairment correlation matrix update is shown in Figure 5. Tentative detected symbol values $s_{det}(n)$ from sequence estimation processor 204 are filtered in filters 500 using channel tap estimates $c_a(\tau)$ and $c_b(\tau)$ from channel tap estimators 202 for antennas a and b to produce expected received

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samples $r_{a, \text{det}}(n)$ and $r_{b, \text{det}}(n)$, respectively. Impairment signal $z_a(n)$ is produced by subtracting, in summing junction **501** $r_{a, \text{det}}(n)$ from the actual received signal samples from antenna a, $r_a(n)$. Similarly, impairment signal $z_b(n)$ is produced by subtracting, in summing junction **502** $r_{b, \text{det}}(n)$ from the actual received signal samples on antenna b, $r_b(n)$. If the tentative detected symbol values are correct and the channel tap estimates are accurate, then error signals $z_a(n)$ and $z_b(n)$ represent the impairment received on antennas a and b respectively. Impairment signals $z_a(n)$ and $z_b(n)$ are scaled by the root of the scaling factor K in multipliers **503** and **505** respectively to produce scaled impairment signals which are coupled to blocks **506** and **507**, respectively.

10 The impairment power received on antenna a, $p_{aa}(n)$, is multiplied in multiplier **511** by the forgetting factor, λ , and summed in junction **510** with the squared magnitude of the scaled impairment signal from block **506** to produce the updated impairment power $p_{aa}(n+1)$. The value of $p_{aa}(n+1)$ is then used to overwrite the memory location **515** of the previous impairment power $p_{aa}(n)$. Similarly, the

15 previous impairment power received on antenna b, $p_{bb}(n)$, is multiplied in multiplier **513** by the forgetting factor, λ , and summed in junction **512** with the squared magnitude of the scaled error signal from block **507** to produce the updated impairment power $p_{bb}(n+1)$ which is used to overwrite the memory location **514** of the previous impairment power $p_{bb}(n)$. To produce the updated impairment cross

20 correlation, the scaled error signal from multiplier **503** is multiplied with the conjugate of the scaled error signal from multiplier **505** in junction **504**. Also, the previous cross-correlation $p_{ab}(n)$, stored in memory **516**, is scaled by the forgetting factor in multiplier **509**. The output of junction **504** is summed in junction **508** with the output of multiplier **509** to yield the updated cross correlation $p_{ab}(n+1)$. As

25 before, the updated value $p_{ab}(n+1)$ is used to overwrite the memory location **516** of the previous value $p_{ab}(n)$.

There is typically a delay in updating the channel tap estimates which allows the tentative detected symbols to become reliable. In U.S. Patent No. 5,164,961 by Gudmundson, et al., incorporated herein by reference in its entirety, this delay is

30 avoided by using multiple channel models: one for each state in the sequence estimation processor **204**. With the present invention, there is also a delay in

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updating the A-matrix quantities. It will be apparent to those skilled in the art that this delay can be avoided by using multiple A-matrices; one for each state in the sequence estimation processor **204**.

5 **B. Description of Embodiment Employing a Selection Processor**

According to the following embodiment the present invention, interference rejection is applied to signals that correspond to N different antenna elements, wherein the N antenna elements are selected from a number $M \geq N$ possible antenna signals. Additionally, these selected antenna element signals may have passed through
10 a specific beamforming process and/or the signals may come from antennas that have different polarizations. As a specific exemplary embodiment, three different cases of multi-element receive antennas are considered which employ the use of horizontal and vertical polarizations. However, other types of orthogonal polarizations may be used, such as plus and minus 45 degrees, or right and left circular.

15 Returning to Figure 1, consider the specific case where there are M antenna elements **104** producing radio signals. Not all M signals will contain information relevant to the transmitted signal. Further, it is desirable to reduce the number of diversity branches sent to the processor **107**. Accordingly, it is beneficial to select a set of N signals most representative of a transmitted symbol sequence.

20 The N channels processed by the processor **107** and generated by the M antennas/antenna elements are described in Figures 6 through 9. Figure 6 shows the first embodiment where M co-phased antenna elements (which may be a combination of both horizontally and vertically polarized elements) given by signals **6010** through **6012** are first passed through a fixed beamforming processor **601** that results in M
25 beam space signals **6020** through **6021**. The antenna elements in this embodiment typically are spaced closely (e.g. a half of a wavelength) together. The selection processor **602** chooses N beam space signals **6022** through **6023** for further IRC processing.

Figure 7 is an embodiment where M co-phased antenna element signals **7001**
30 through **7004** are passed through two beamforming processors **701** and **702**, one each for the vertically and horizontally polarized elements. Signals **7001** through **7002**

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correspond to the vertical antenna elements and are processed by 701 giving outputs 7011 through 7012, while signals 7003 through 7004 correspond to the horizontal antenna elements and are processed by 702 giving outputs 7021 through 7022. Signals 7011 through 7012 and 7021 through 7022 are processed by the selection processor 703 and N output signals 7030 through 7031 are selected.

Figure 8 is an embodiment that uses sector antennas, where the antennas may be either vertically or horizontally polarized. The antenna signals are 8000 through 8003 and are processed by the selection processor 801 to generate N output signals 8010 through 8011. In this embodiment, antennas with the same polarization may be physically separated (e.g. 10-20 wavelengths).

To reiterate, the embodiments shown in Figures 6-8 are not restricted to the use of horizontal and vertical polarizations. As noted, other types of orthogonal polarizations may be used, such as plus and minus 45 degrees, or right and left circular. Furthermore, in the embodiment disclosed in Figure 7, more than two beam processors may be employed. For instance, different beam processors may be assigned to process groups of signals originating from different spatially separated groups of antenna elements.

Figure 9 shows an embodiment of the branch selection processor. Each input signal branch 9000 through 9001 is first filtered by 901 through 902 and then passed through some signal quality measure device 903 through 904 which generates measures 9030 through 9040 that is used to compare the signal's quality relative to the other signals. The M signals 9010 through 9020 are sent to the selection multiplexor 905, which chooses the N signals (out of M) that have the best measure 9030 through 9040. The measure criteria may be defined to represent one or more of the following qualities: measured instantaneous branch power; measured average branch power; beam center direction relative to desired signal direction; signal quality as measured from sync word (measured $(S+N)/N$). "S" denotes signal power, whereas "N" denotes impairment power.

Furthermore, the selection may be constrained to keeping at least one vertically polarized and one horizontally polarized signal. For example, choosing the horizontal beam with the maximum power and the vertical beam with the maximum

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power performs best in certain circumstances (such as the presence of Rayleigh fading). Again, other types of orthogonal signals may be used.

Still a further embodiment may dispense with the selection processor altogether. In this case, the processor 107 is fed all of the M signals received from the antenna elements. This embodiment may employ antenna elements producing
 5 orthogonally polarized signals and/or one or more fixed beam processors as discussed above.

C. Description of Embodiment having One Antenna and a Scalar Branch Metric Processor

10 In an alternative embodiment of the present invention, interference rejection is applied to signals that correspond to different phase references. Normally, the in-phase (I) and quadrature (Q) components of the baseband signal are combined into one complex signal. However, when the interference is not rotationally invariant, then the two components must be treated as separate, scalar received signals. See, for
 15 example, B. Picinbono, "On circularity", IEEE Trans. Sig. Proc., Vol. 42, pp. 3473-3482, Dec. 1994.

As a specific embodiment, the case of a single receive antenna is considered, though it will be apparent to those skilled in the art how multiple receive antennas, beams, or polarizations would be incorporated. With a single receive antenna,
 20 complex receive samples $r(n)$ are split into in-phase samples $I(n)$ and quadrature samples $Q(n)$. These two sample streams are treated as if they came from two, scalar channels. The new branch metric is then

$$M_h(n) = \mathbf{v}_h^T(n) \mathbf{A}(n) \mathbf{v}_h(n)$$

-25 where

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$$\mathbf{v}_h(n) = [v_{h,I}(n) \quad v_{h,Q}(n)]^T = [\operatorname{Re}\{e_h(n)\} \quad \operatorname{Im}\{e_h(n)\}]^T$$

$$e_h(n) = r(n) - \mathbf{c}(n) \mathbf{s}_h(n)$$

$$\mathbf{c}(n) = [c(0;n) \quad c(1;n) \quad \dots \quad c(N_t-1;n)]$$

$$\mathbf{s}_h(n) = [s_h(n) \quad s_h(n-1) \quad \dots \quad s_h(n-N_t+1)]^T$$

$$\mathbf{A}(n) = \mathbf{R}_{ww}^{-1}(n)$$

$$\mathbf{R}_{ww}(n) = E\{\mathbf{w}(n)\mathbf{w}^T(n)\}$$

$$\mathbf{w}(n) = [\operatorname{Re}\{z(n)\} \quad \operatorname{Im}\{z(n)\}]^T$$

and $z(n)$ is the complex, additive impairment. Superscript "T" denotes transpose.

The vector $\mathbf{w}(n)$ is the corresponding scalar impairment vector. The channel tap estimates are denoted $c(\tau)$, and there are N_t of them. The real matrices $\mathbf{A}(n)$ and

- 5 $\mathbf{R}_{ww}^{-1}(n)$ are specific examples of scalar impairment correlation properties of which other forms are known. Throughout the following, the term A-matrix is used generically to refer to any estimate of the impairment correlation properties.

The A-matrix can be estimated and tracked in a variety of ways. One way is to form impairment samples $z(n)$ by subtracting expected received samples from the
 10 actual received samples. Scalar impairment vector $\mathbf{w}(n)$ is then given by the equation given above. A straightforward way of forming the A-matrix is given by:

$$\mathbf{R}_{ww}(n) = \lambda \mathbf{R}_{ww}(n-1) + \mathbf{w}(n)\mathbf{w}^T(n)$$

$$\mathbf{A}(n) = \mathbf{R}_{ww}^{-1}(n)$$

To reduce complexity, the matrix inversion lemma may be used so that the A-matrix can be updated directly as

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$$\mathbf{A}(n) = \frac{1}{\lambda} [\mathbf{A}(n-1) - \frac{\mathbf{p}(n)\mathbf{p}^T(n)}{\lambda + \mathbf{w}^T(n)\mathbf{p}(n)}]$$

$$\mathbf{p}(n) = \mathbf{A}(n-1)\mathbf{w}(n)$$

Because the A-matrix is symmetric, only the elements on the diagonal and above need be computed.

For the case of one receive channel, the branch metric can be expressed:

$$M_h(n) = m_{II}(v_{h,I}(n))^2 + m_{QQ}(v_{h,Q}(n))^2 + m_{IQ}v_{h,I}(n)v_{h,Q}(n)$$

Also, the impairment correlations can be estimated using:

$$p_{II}(n+1) = \lambda p_{II}(n) + v_I^2(n)$$

$$p_{QQ}(n+1) = \lambda p_{QQ}(n) + v_Q^2(n)$$

$$p_{IQ}(n+1) = \lambda p_{IQ}(n) + v_I(n)v_Q(n)$$

- 5 where $v_I(n)$ and $v_Q(n)$ are the real and imaginary parts of an impairment sample estimate.

With these estimates, the combining weights can be computed as:

$$m_{II} = K p_{II}(n)$$

$$m_{QQ} = K p_{QQ}(n)$$

$$m_{IQ} = -2K p_{IQ}(n)$$

Ideally, the scaling factor K would be given by:

$$K = \frac{1}{p_{II}(n)p_{QQ}(n) - p_{IQ}^2(n)}$$

However, other values are possible, including unity, so that no scaling is necessary.

The alternative embodiment is illustrated by the processor given in Figure 10. After radio processing and initial analog-to-digital conversion (not shown), the received signal is coupled to a signal pre-processor or sync, block **1002**, where timing and synchronization information are determined, producing synchronized complex
 5 received samples $r(n)$. Channel tap estimator **1004** produces channel tap estimates $c(\tau)$ which model the fading, dispersive channel. These channel tap estimates are coupled to scalar branch metric processor **1006**.

Also coupled to scalar branch metric processor **1006** is an estimate of the scalar impairment correlation properties obtained from impairment correlation
 10 estimator **1008**. The estimate of the impairment correlation properties includes information regarding the impairment correlation properties between the I and Q components of the received signal, which are scalar quantities.

Scalar branch metric processor **1006** uses the received signal samples $r(n)$, channel tap estimates $c(\tau)$, and an estimate of the impairment correlation properties to
 15 form branch metric $M_h(n)$. This branch metric is used in sequence estimation processor **1010** to develop tentative and final estimates of the transmitted symbols.

A specific embodiment of the scalar branch metric processor **1006** is illustrated in Figure 11. A symbol sequence generator **1124** generates hypothesized symbol sequences $s_h(n)$. These sequences are filtered by filter **1104** using channel estimates
 20 $c(\tau)$ to produce hypothesized received signal samples. The hypothesized received signal samples are subtracted from the actual received signal samples in summing junction **1102** to produce complex error signals. The real filter **1108** only passes the real part (in-phase component) of the complex error signals, and the image filter **1106** only passes the imaginary part (quadrature component) of the complex error signals.
 25 The real part of the error signal is squared in block **1110** then multiplied by multiplier m_{II} in block **1132**, the result being coupled to summing junction **1116**. Similarly, the imaginary part of the error signal is squared in block **1118** then multiplied by multiplier m_{QQ} in block **1114**, the result being coupled to summing junction **1116**. Also, the real and imaginary parts of the error signal are multiplied together in block

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1134, multiplied by multiplier m_{IQ} in block 1112, then coupled to summing junction 1116. The output of summing junction 1116 is the branch metric $M_n(n)$.

A specific embodiment of the scalar impairment correlation estimator is illustrated in Figure 12. Known or tentatively detected symbol values from sequence
 5 estimating processor 1010 are filtered by filter 1232 using channel tap estimates $c(\tau)$ from channel tap estimator 1004 to produce estimated received samples. Impairment samples are produced by subtracting estimated received samples from actual received samples in summing junction 1202. The real filter 1204 only passes the real parts (in-phase components) of the impairment samples, and the image filter 1206 only passes
 10 the imaginary parts (quadrature components) of the impairment samples. The in-phase components of the impairment samples are squared in block 1220 and provided to summing junction 1228. Also, the in-phase impairment power estimate p_{II} , stored in memory 1224, is scaled in junction 1222 by scale factor λ and provided to summing junction 1228. The output of junction 1228 gives the updated power
 15 estimate, which is written into memory 1224. Similarly, the quadrature components of the impairment samples are squared in block 1210 and provided to summing junction 1212. Also, the quadrature impairment power estimate p_{QQ} , stored in memory 1208, is scaled in junction 1214 by scale factor λ and provided to summing junction 1212. The output of junction 1212 gives the updated power estimate, which
 20 is written into memory 1208. Finally, the in-phase and quadrature components of the impairment samples are multiplied together in block 1250 and provided to summing junction 1216. Also, the in-phase/quadrature cross-correlation estimate p_{IQ} , stored in memory 1218, is scaled in junction 1230 by scale factor λ and provided to summing junction 1216. The output of junction 1216 gives the updated cross-correlation
 25 estimate, which is written into memory 1218.

Per-Survivor processing techniques can be used to improve performance. For example, there can be one or more sets of channel tap estimates and impairment correlation estimates per state in the sequence estimation processor. This allows immediate updating of estimates, without the need for a decision delay to obtain
 30 reliable tentatively detected symbols.

Also, all of the techniques discussed in section B (above) can be employed here to cull out a number of N signals from a larger number of M signals prior to performing interference rejection combining using a scalar branch matrix processor.

It will be known to those skilled in the art how the present invention can be
 5 used in conjunction with fractionally-spaced equalization as well as in conjunction with nonadaptive scenarios.

D. Description of Embodiment Employing Hybrid Combining

According to the following embodiment of the present invention, interference rejection is applied to sets of signals. The resulting metrics are then simply added
 10 together, with a possible weighting prior to adding. This trades performance for a reduction in complexity. The selection criteria can be adaptive, based on impairment correlation measurements, signal strength measurements, or other criteria. Also, the selection may be fixed.

Figure 13 is an embodiment of processor 107 from Figure 1, where 2 antennas
 15 and fractionally-spaced sampling by a factor of 2 are used. Thus, for each antenna, two symbol-spaced data sequences are formed, corresponding to two sampling phases. Sync blocks 1302 and 1304 take the oversampled signal streams from antennas a and b and produce two symbol-spaced sample streams each. Denoting the antennas with subscripts a and b and the sampling phases with subscripts 0 and 1, the four resulting
 20 received signal sample sequences are denoted $r_{a0}(n)$, $r_{a1}(n)$, $r_{b0}(n)$ and $r_{b1}(n)$. The embodiment uses a fixed selection criteria, so that interference rejection is applied to the pair $\{r_{a0}(n), r_{b0}(n)\}$ and the pair $\{r_{a1}(n), r_{b1}(n)\}$.

So, received signal sample streams $r_{a0}(n)$ and $r_{b0}(n)$ are provided to branch metric processor 1306. Also provided to branch metric processor 1306 are channel
 25 tap estimates corresponding to streams $r_{a0}(n)$ and $r_{b0}(n)$, which are computed in channel tap estimators 1310 and 1312. Impairment correlation estimates corresponding to streams $r_{a0}(n)$ and $r_{b0}(n)$ are provided by impairment correlation estimator 1314.

Similarly, received signal sample streams $r_{a1}(n)$ and $r_{b1}(n)$ are provided to
 30 branch metric processor 1308. Also provided to branch metric processor 1308 are channel tap estimates corresponding to streams $r_{a1}(n)$ and $r_{b1}(n)$, which are computed

in channel tap estimators 1316 and 1318. Impairment correlation estimates corresponding to streams $r_{s1}(n)$ and $r_{s2}(n)$ are provided by impairment correlation estimator 1320.

5 The branch metrics from branch metric processors 1306 and 1308 are summed in added 1322, which produces a combined branch metric. The combined branch metric is then provided to sequence estimation processor 1324, which develops tentative and final estimates of the transmitted symbol sequence.

10 Although exemplary embodiments of the present invention have been described and illustrated herein to facilitate understanding of the present invention, it should be understood that the present invention is not limited thereto since modifications may be made by persons skilled in the art. The present application contemplates any and all such modifications that fall within the scope of the underlying invention disclosed and claimed herein.

"comprises/comprising" when used in this specification is taken to specify the presence of stated features, integers, steps or components but does not preclude the presence or addition of one or more other features, integers, steps, components or groups thereof.



THE CLAIMS DEFINING THE INVENTION ARE AS FOLLOWS:

1. A method for reducing the effects of signal fading, time dispersion, and interference in a radio communications system, including the steps of:

(a) receiving a radio signal on at least one antenna element representing a transmitted symbol sequence;

(b) processing said radio signal to produce received signal samples for said at least one antenna;

(c) estimating a channel tap for said at least one antenna to produce a channel tap estimate;

(d) estimating scalar impairment correlation properties among the received signal samples to produce an estimate of scalar impairment correlation properties;

(e) forming scalar branch metrics in a scalar branch metric processor using said received signal samples, said channel tap estimate, and said scalar estimate of impairment correlation properties; and

(f) employing said scalar branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.

2. A method according to claim 1, in which said forming step (e) includes:

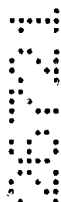
(g) generating hypothetical symbol sequences;

(h) filtering said hypothetical signal sequences with said channel tap estimate to produce hypothesized received signal samples for said at least one antenna;

(i) subtracting said hypothesized received signal samples from the received signal samples to produce complex error signals; and

(j) processing said complex error signals with said scalar estimate of impairment correlation properties to produce branch metrics.

3. A method according to claim 2, in which said forming step (j) further includes:



(k) extracting an in-phase phase component from said complex error signal, and extracting a quadrature component from said complex error signal;

(l) processing said in-phase phase component and said quadrature component to produce said branch metrics.

4. A method according to claim 1, in which said estimating step (d) includes:

(g) generating tentative detected symbol sequences;

(h) filtering said tentative detected symbol sequences with said scalar channel tap estimate to produce estimated received signal samples for said at least one antenna;

(i) subtracting said estimated received signal samples from the received signal samples to produce impairment signal samples; and

(j) processing said impairment signal samples with said estimate of scalar impairment correlation properties to produce an updated estimate of said scalar impairment correlation properties.

5. A method according to claim 4, in which said forming step (j) further includes:

(k) extracting an in-phase phase component from said impairment signal samples, and extracting a quadrature component of said impairment signal samples;

(l) processing said in-phase component and said quadrature component to produce said updated estimate of said scalar correlation properties.

6. An apparatus for reducing the effects of signal fading, time dispersion, and interference in a radio communications system, including:

means for receiving a radio signal on at least one antenna element representing a transmitted symbol sequence;

means for processing said radio signal to produce received signal samples for said at least one antenna;

means for estimating a channel tap for said at least one antenna to produce a channel tap estimate;



means for estimating scalar impairment correlation properties among said radio signal samples to produce an estimate of scalar impairment correlation properties;

means for forming scalar branch metrics in a scalar branch metric processor using said received signal samples, said channel tap estimates, and said scalar estimate of impairment correlation properties; and

means for employing said scalar branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.

7. An apparatus according to claim 6, in which said means for forming scalar branch matrices includes:

means for generating hypothetical symbol sequences;

means for filtering said hypothetical signal sequences with said channel tap estimate to produce hypothesized received signal samples for said at least one antenna;

means for subtracting said hypothesized received signal samples from the received signal samples to produce complex error signals; and

means for processing said complex error signals with said scalar estimate of impairment correlation properties to produce branch metrics.

8. An apparatus according to claim 7, in which said forming means for processing said complex error signals further includes:

means for extracting an in-phase phase component from said complex error signal, and extracting a quadrature component from said complex error signal;

means for processing said in-phase phase component and said quadrature component to produce said branch metrics.

9. An apparatus according to claim 6, in which said means for estimating scalar impairment correlation properties includes:

means for generating tentative detected symbol sequences;



means for filtering said tentative detected symbol sequences with said scalar channel tap estimate to produce estimated received signal samples for said at least one antenna;

means for subtracting said estimated received signal samples from the received signal samples to produce impairment signal samples; and

means for processing said impairment signal samples with said estimate of scalar impairment correlation properties to produce an updated estimate of said scalar impairment correlation properties.

10. An apparatus according to claim 9, in which said means for processing said impairment signal samples further includes:

means for extracting an in-phase phase component from said impairment signal samples, and extracting a quadrature component from said impairment signal samples;

means for processing said in-phase phase component and said quadrature component to produce said updated estimate of said scalar correlation properties.

11. A method for reducing degradation in a transmitted signal sequence including the step of:

(a) receiving a number of M radio signals representing said transmitted signal sequence;

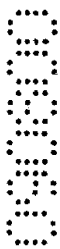
(b) selecting a number of N signals from said number of M radio signals using a selection processor on the basis of one or more selection criterion, where $N \leq M$;

(c) processing said N signals to generate an estimate of said transmitted signal sequence.

12. The method of claim 11, wherein step (a) further includes:

(d) receiving said M radio signals from M co-phased antenna elements;

(e) processing said M radio signals using a fixed beamforming processor.



13. The method of claim 12, wherein said M antenna elements include at least one element from each of two orthogonal polarisations.

14. The method of claim 11, wherein step (a) further includes:

(d) receiving said M radio signals from M antenna elements, wherein said M antenna elements form a plurality of groupings of antenna elements;

(e) processing said M radio signals using a plurality of beamforming processors, wherein each beamforming processor is associated with one of said groupings of antenna elements.

15. The method of claim 14, wherein a collection of antenna elements having a first polarisation form a first grouping, and a collection of antenna elements having a second polarisation form a second grouping, further wherein said first polarisation is orthogonal to said second polarisation.

16. The method of claim 14, wherein a first collection of spatially associated antenna elements form a first grouping, and a second collection of spatially associated antenna elements form a second grouping.

17. The method of claim 11, wherein step (a) further includes:

(d) receiving said M radio signals from at least one sector antenna.

18. The method of claim 11, wherein said criterion is one or more criterion from the following group of criteria: instantaneous power of a signal; average power of a signal; beam center direction relative to a desired signal direction; and signal quality as measured from a sync word.

19. The method of claim 11, wherein said step (b) is constrained to select at least one signal having a first polarisation, and at least one signal having a second polarisation, wherein the first polarisation is orthogonal to said second polarisation.



20. The method of claim 11, wherein said step (c) further includes the steps of:

- (d) receiving said N signals from said selection processor;
- (e) processing said N signals to produce received signal samples for N antennas;
- (f) estimating channel taps for said N antennas to produce channel tap estimates;
- (g) estimating impairment correlation properties among said received signals to produce an estimate of impairment correlation properties;
- (h) forming branch metrics in a branch metric processor using said received signal samples, said channel tap estimates, and said estimate of impairment correlation properties; and
- (i) employing said scalar branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.

21. The method of claim 11, wherein said step (c) further includes the steps of:

- (a) receiving said N signals from said selection processor;
- (b) processing said N signals to produce received signal samples for N antennas;
- (c) estimating channel taps for said N antennas to produce channel tap estimates;
- (d) estimating scalar impairment correlation properties among said received signals to produce an estimate of scalar impairment correlation properties;
- (e) forming scalar branch metrics in a scalar branch metric processor using said received signal samples, said channel tap estimates, and said estimate of scalar impairment correlation properties; and
- (f) employing said scalar branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.

22. An apparatus for reducing degradation in a transmitted signal sequence including:



(a) means for receiving a number of M radio signals representing said transmitted signal sequence;

(b) means for selecting a number of N signals from said number of M radio signals using a selection processor on the basis of one or more selection criterion, where $N \leq M$;

(c) means for processing said N signals to generate an estimate of said transmitted signal sequence.

23. The apparatus of claim 22, wherein said means for receiving further includes:

means for receiving said M radio signals from M co-phased antenna elements;

means for processing said M radio signals using a fixed beamforming processor.

24. The apparatus of claim 23, wherein said M antenna elements include at least one element from each of two orthogonal polarisations.

25. The apparatus of claim 22, wherein said means for receiving further includes:

M antenna elements for receiving a corresponding M signals, wherein said M antenna elements form a plurality of groupings of antenna elements;

a plurality of beamforming processors, each beamforming processor associated with one of said groupings of antenna elements.

26. The apparatus of claim 25, wherein a collection of antenna elements having a first polarisation form a first grouping, and a collection of antenna elements having a second polarisation form a second grouping, further wherein said first polarisation is orthogonal to said second polarisation.



27. The apparatus of claim 25, wherein a first collection of spatially associated antenna elements form a first grouping, and a second collection of spatially associated antenna elements form a second grouping.

28. The apparatus of claim 22, wherein means for receiving further includes:
means for receiving said M radio signals from at least one sector antenna.

29. The apparatus of claim 22, wherein said criterion is one or more criterion from the following group of criteria: instantaneous power of a signal; average power of a signal; beam centre direction relative to a desired signal direction; and signal quality as measured from a sync word.

30. The apparatus of claim 22, wherein said means for selecting is constrained to select at least one signal having a first polarisation and at least one signal having a second polarisation, wherein said first polarisation is orthogonal to said second polarisation.

31. The apparatus of claim 22, wherein said means for processing further includes:

means for receiving said N signals from said selection processor;

means for processing said N signals to produce received signal samples for N antennas;

means for estimating channel taps for said N antennas to produce channel tap estimates;

means for estimating impairment correlation properties among said received signals to produce an estimate of impairment correlation properties;

means for forming branch metrics in a branch metric processor using said received signal samples, said channel tap estimates, and said estimate of impairment correlation properties; and

means for employing said scalar branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.



32. The apparatus of claim 22, wherein said means for processing further includes:

means for receiving said N signals from said selection processor;

means for processing said N signals to produce received signal samples for N antennas;

means for estimating channel taps for said N antennas to produce channel tap estimates;

means for estimating scalar impairment correlation properties among said received signals to produce an estimate of scalar impairment correlation properties;

means for forming scalar branch metrics in a scalar branch metric processor using said received signal samples, said channel tap estimates, and said estimate of scalar impairment correlation properties; and

means for employing said scalar branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.

33. The method of claim 11, wherein said M antenna elements include at least one element having a first polarisation, and at least one other antenna element having a second polarisation.

34. The method of claim 33, wherein said first and second polarisations are orthogonal to each other.

35. The method of claim 34, wherein said orthogonal first and second polarisations are: i) horizontal and vertical polarisations, respectively; ii) plus and minus 45 degree polarisations, respectively; or iii) right and left circular polarisations, respectively.

36. The apparatus of claim 22, wherein:

said means for receiving includes M antenna elements, wherein said M antenna elements include at least one element having a first polarization, and at least one other antenna element having a second polarization;



said means for selecting includes a selector; and
 said means for processing includes processing logic.

37. The apparatus of claim 36, wherein said first and second polarisations are orthogonal to each other.

38. The apparatus of claim 37, wherein said orthogonal first and second polarisations are: i) horizontal and vertical polarisations, respectively; ii) plus and minus 45 degree polarisations, respectively; or iii) right and left circular polarisations, respectively.

39. A method for reducing the effects of signal fading, time dispersion, and interference in a radio communications system, including the steps of:

- (a) receiving a signal representing a transmitted symbol sequence on M antenna elements;
- (b) processing said signal to produce received signal samples for each of said M antenna elements;
- (c) estimating channel taps for said M antenna elements to produce channel tap estimates;
- (d) estimating impairment correlation properties among said received signals to produce an estimate of impairment correlation properties;
- (e) forming branch metrics in a branch metric processor using said received signal samples, said channel tap estimates, and said estimate of impairment correlation properties; and
- (f) employing said branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence,

wherein said M antenna elements include at least a first element producing a first polarisation, and a second element producing a second polarisation.

40. The method of claim 39, wherein said processing step (b) includes processing said radio signal using at least one fixed beamforming processor.



41. An apparatus for reducing the effects of signal fading, time dispersion, and interference in a radio communications system, including:

M antenna elements for receiving a signal representing a transmitted symbol sequence;

processing logic for processing said signal to produce received signal samples for each said M antenna elements;

a first estimator for estimating channel taps for said M antenna elements to produce channel tap estimates;

a second estimator for estimating impairment correlation properties among said received signals to produce an estimate of impairment correlation properties;

a branch metric processor for forming branch metrics using said received signal samples, said channel tap estimates, and said estimate of impairment correlation properties; and

logic for employing said branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence,

wherein said M antenna elements include at least a first element producing a first polarisation, and a second element producing a second polarisation.

42. The apparatus of claim 41, wherein said processing logic employs at least one fixed beamforming processor.

43. In a digital communications system for transmitting a sequence of digital symbols, a method for reducing the effects of signal fading, time dispersion, and interference in a radio communications system, including the steps of:

- (a) receiving a number of M radio signals;
- (b) selecting groups of radio signals using a selection processor;
- (c) processing each group of radio signals to produce branch metrics;
- (d) adding said branch metrics from different groups to produce combined branch metrics;
- (e) employing said combined branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.



44. The method according to claim 43, in which processing step (c) is applied to each of said groups of radio signals, and further includes, for each of said groups, the steps of:

- (f) receiving a group of radio signals from said selection processor;
- (g) processing said group of signals to produce received signal samples;
- (h) estimating channel taps for said group of signals to produce channel tap estimates;
- (i) estimating impairment correlation properties among the signals within the group to produce an estimate of impairment correlation properties.
- (j) forming branch metrics in a branch metric processor using said received signal samples, said channel tap estimates, and said estimate of impairment correlation properties.

45. An apparatus for reducing the effects of signal fading, time dispersion, and interference in a radio communications system, including:

means for receiving a number of M radio signals representing a transmitted sequence of symbols;

means for selecting groups of radio signals using a selection processor;

a plurality of processing means, each for processing a respective group of radio signals, to produce branch metrics;

means for adding said branch metrics from different groups to produce combined branch metrics;

means for employing said combined branch metrics in a sequence estimation algorithm to estimate said transmitted symbol sequence.

46. The apparatus according to claim 45, in which each one of said plurality of processing means includes:

means for receiving said group of radio signals to produce received signal samples;

means for processing said group of signals to produce received signal samples;



means for estimating channel taps for said group of signals to produce channel tap estimates;

means for estimating impairment correlation properties among the signals within the group to produce an estimate of impairment correlation properties; and

means for forming branch metrics in a branch metrics processor using said received signals samples, said channel tap estimates, and said estimate of impairment correlation properties.

47. A method as claimed in claim 1, 11, 39 or 43, substantially as hereinbefore described with reference to figures 2, 4, and 10 to 13 of the accompanying drawings.

48. An apparatus as claimed in any one of claims 6, 22, 41 or 45, substantially as hereinbefore described with reference to figures 2, 4, and 10 to 13 of the accompanying drawings.

DATED 30th July 2000

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2ND FLOOR, "THE GLASSHOUSE"
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HAWTHORN VIC 3122
AUSTRALIA



FIG. 1

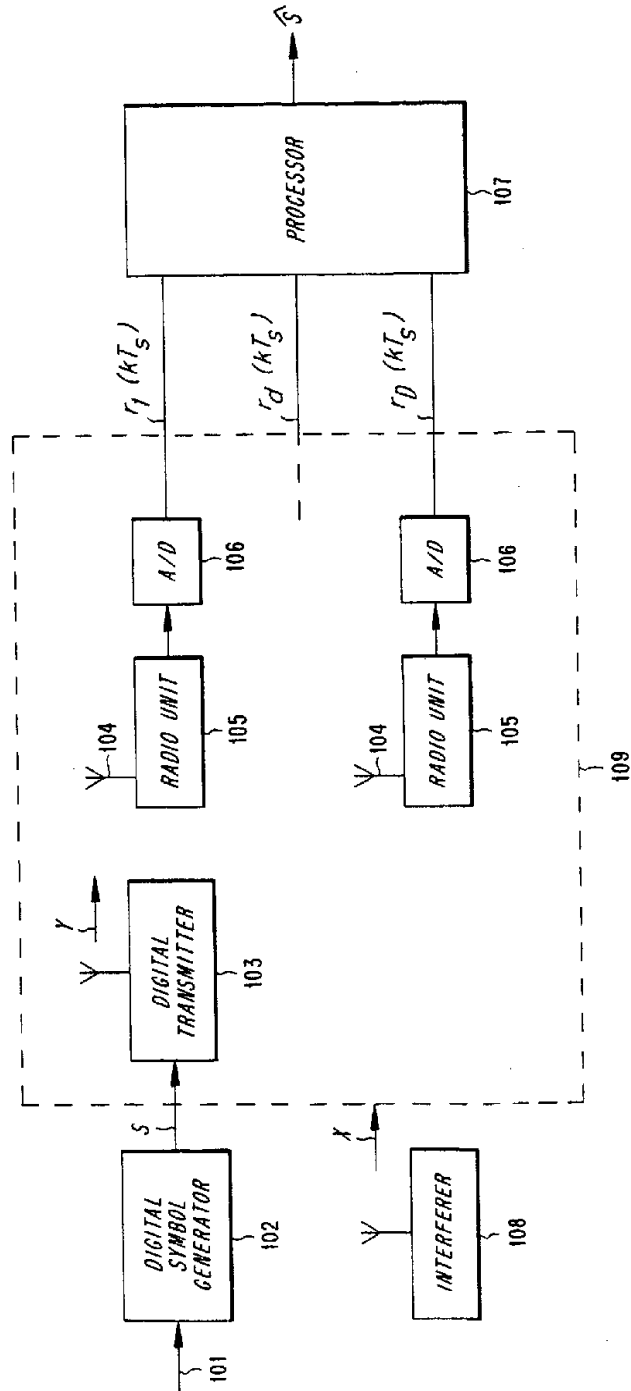


FIG. 2

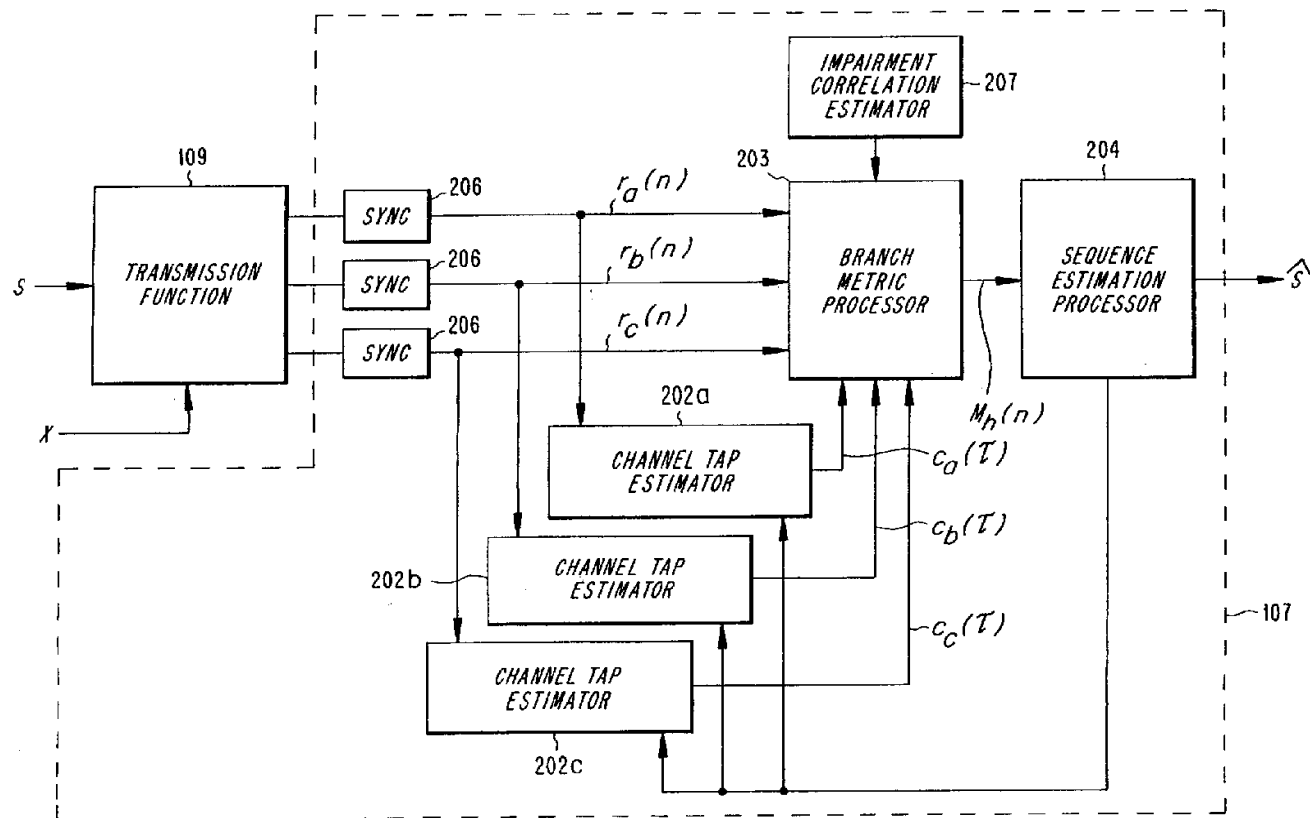


FIG. 3

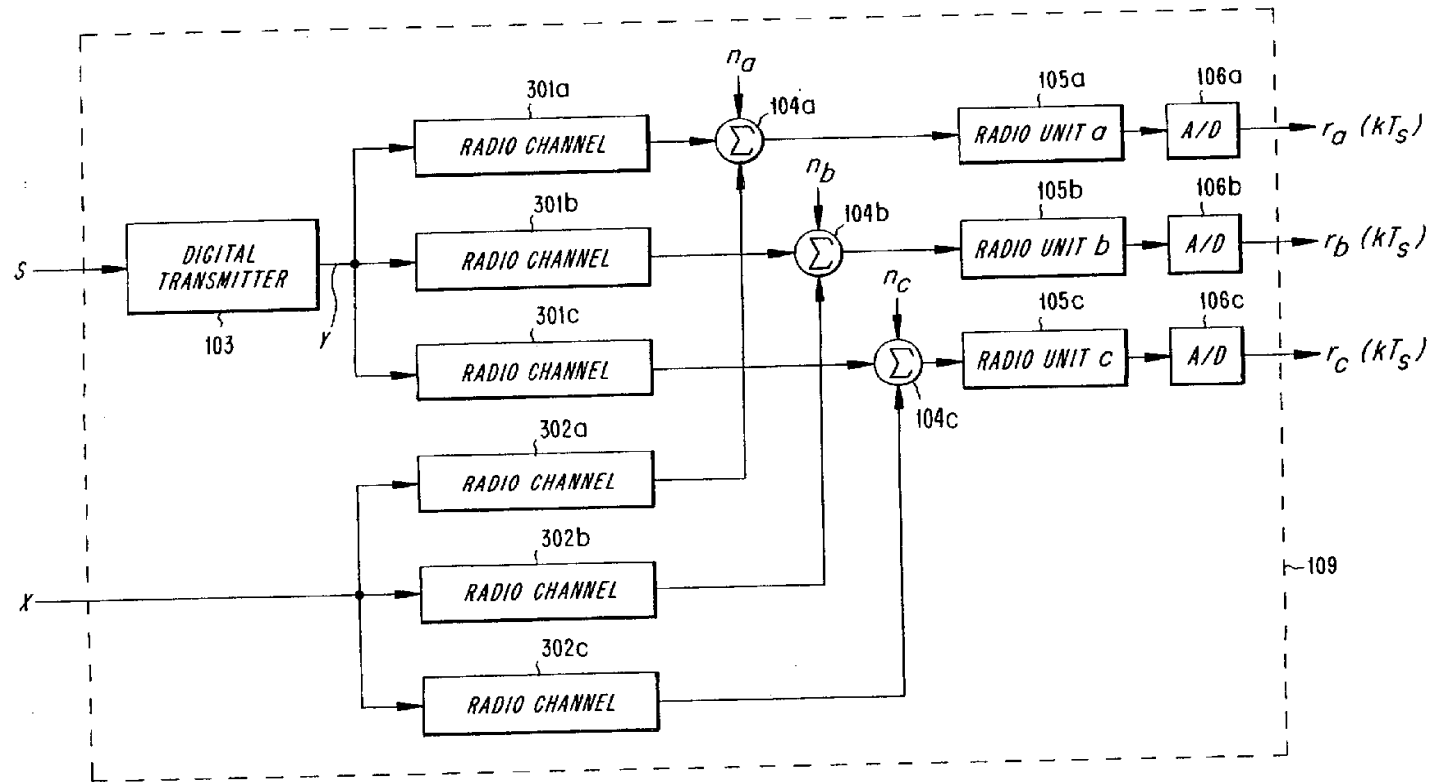
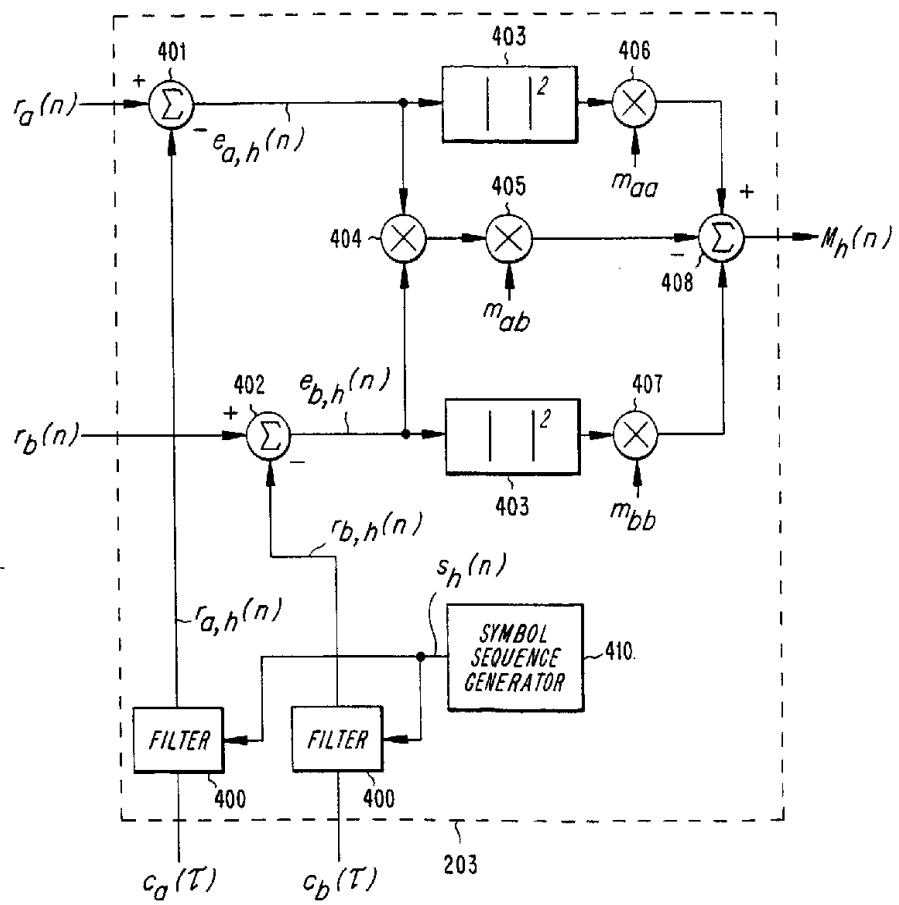


FIG. 4



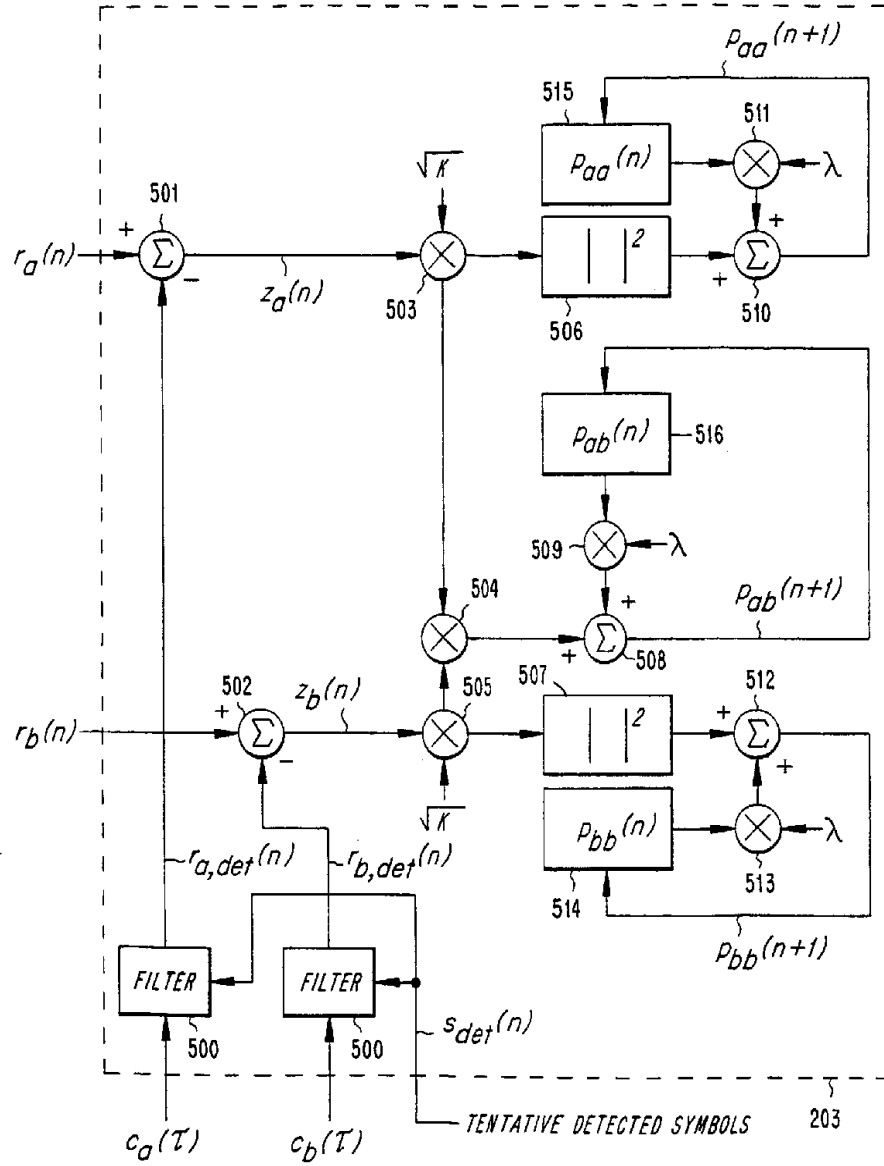


FIG. 5

FIG. 6

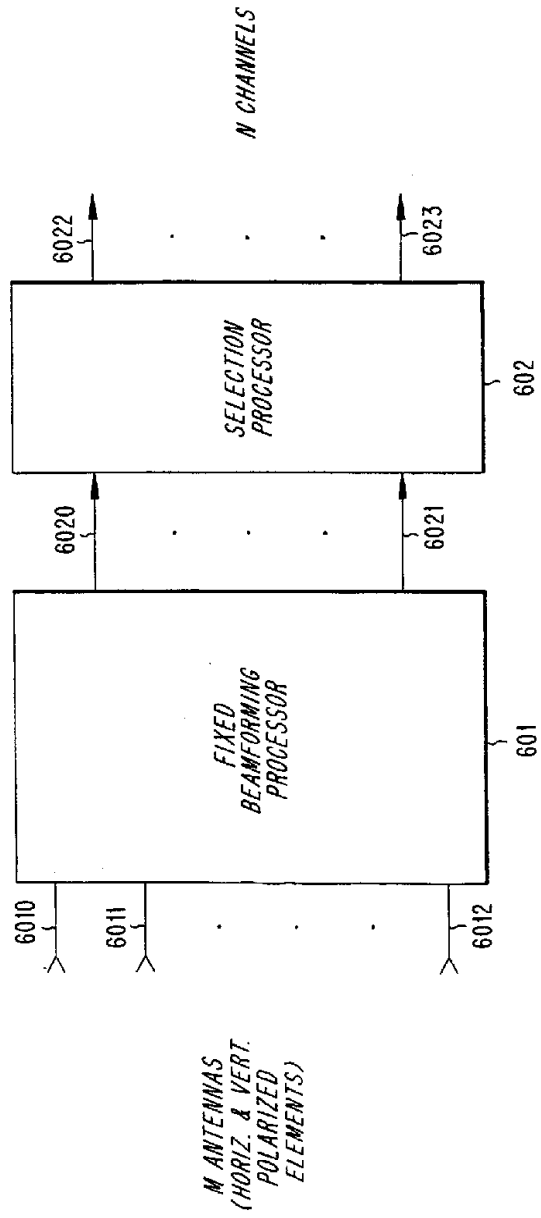
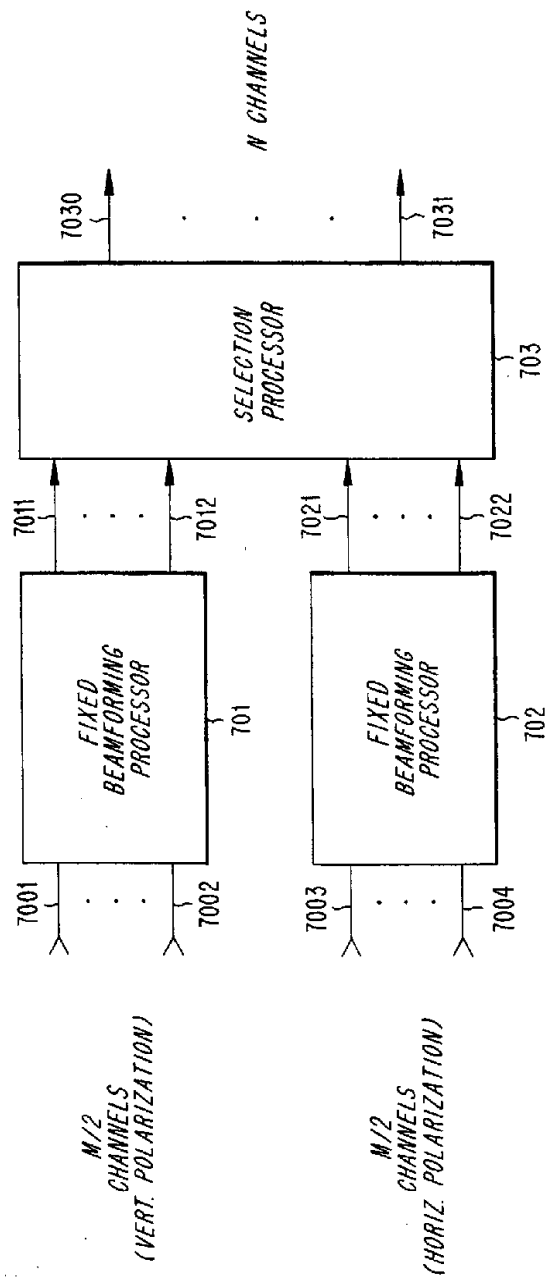


FIG. 7



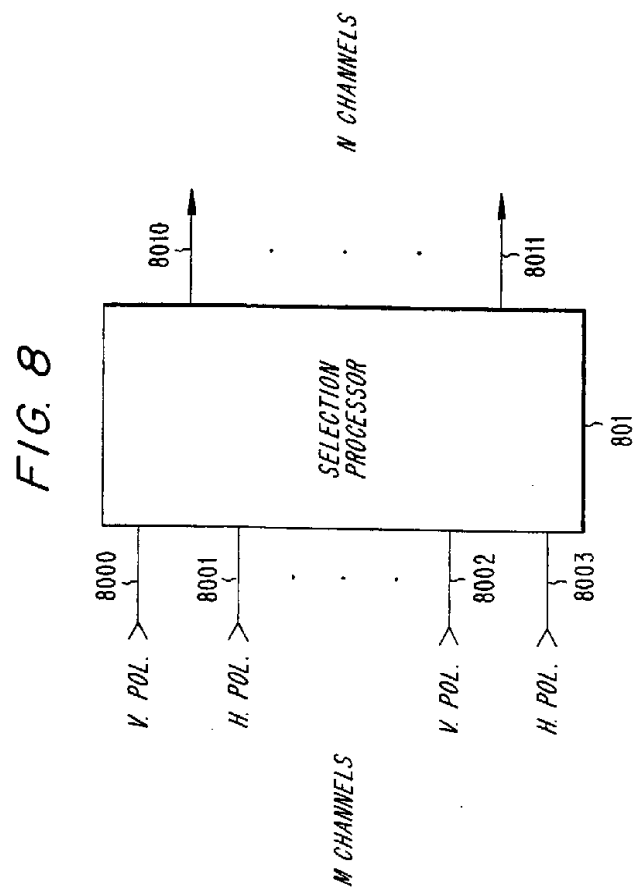
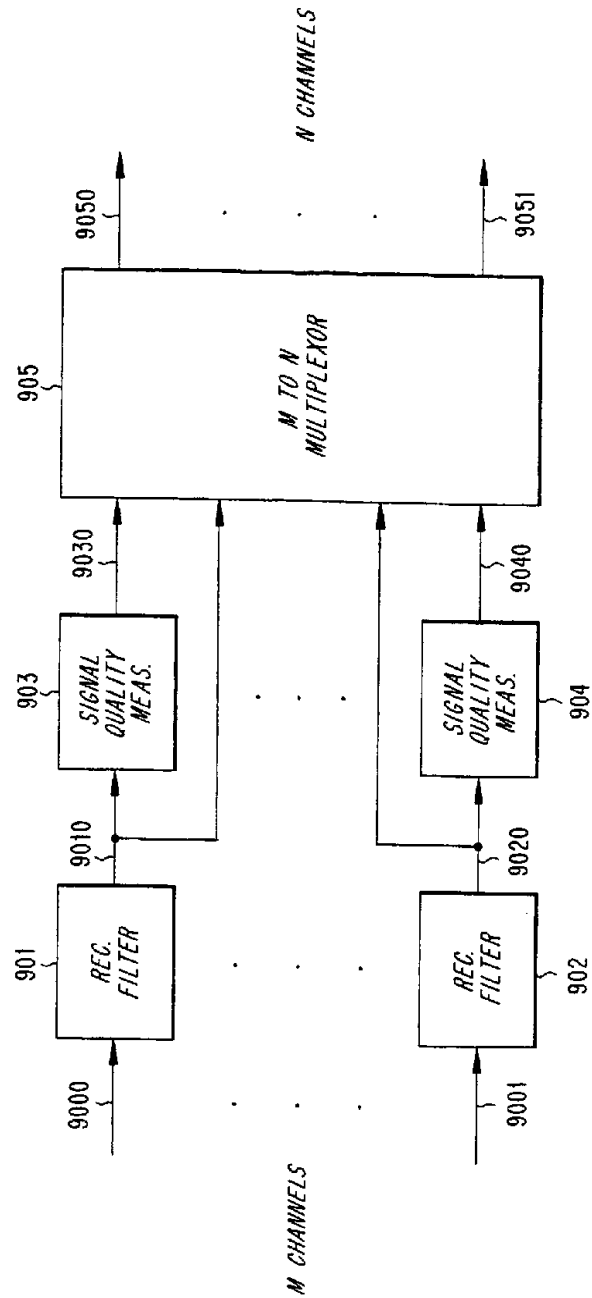
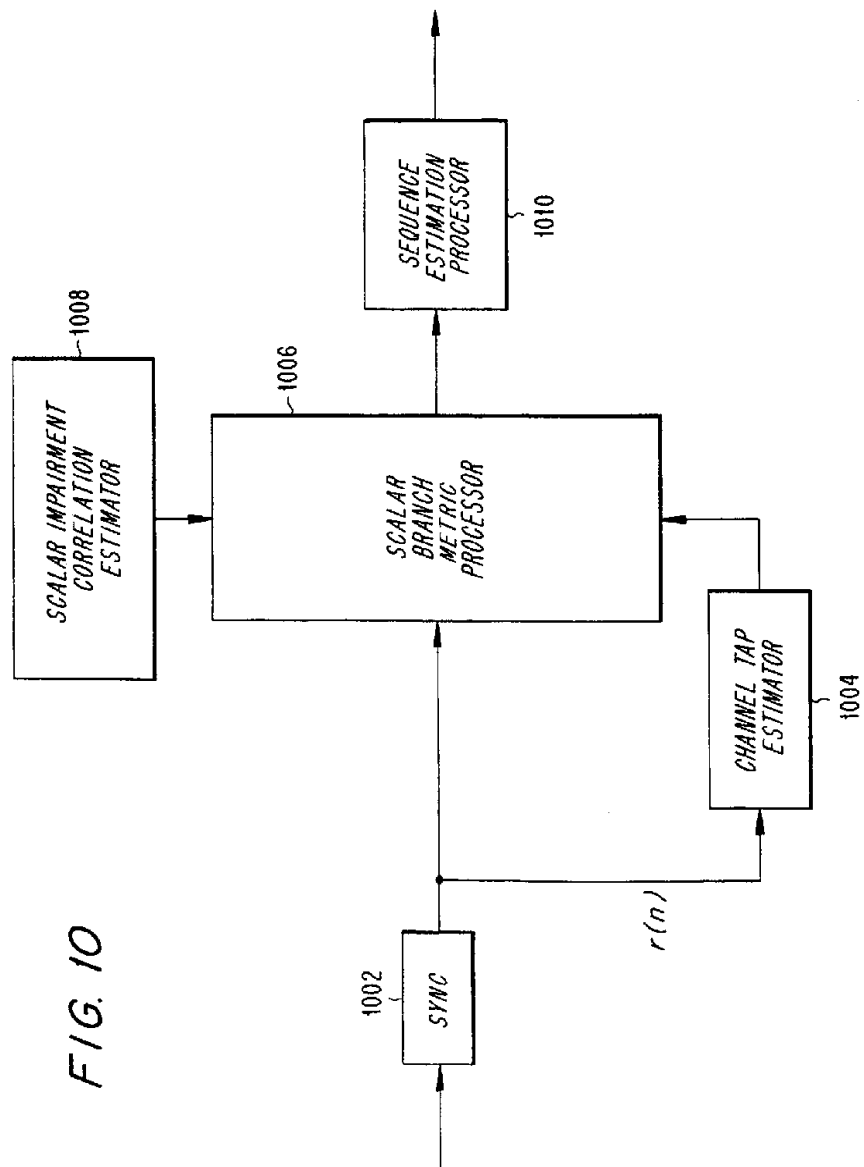


FIG. 9



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FIG. 11

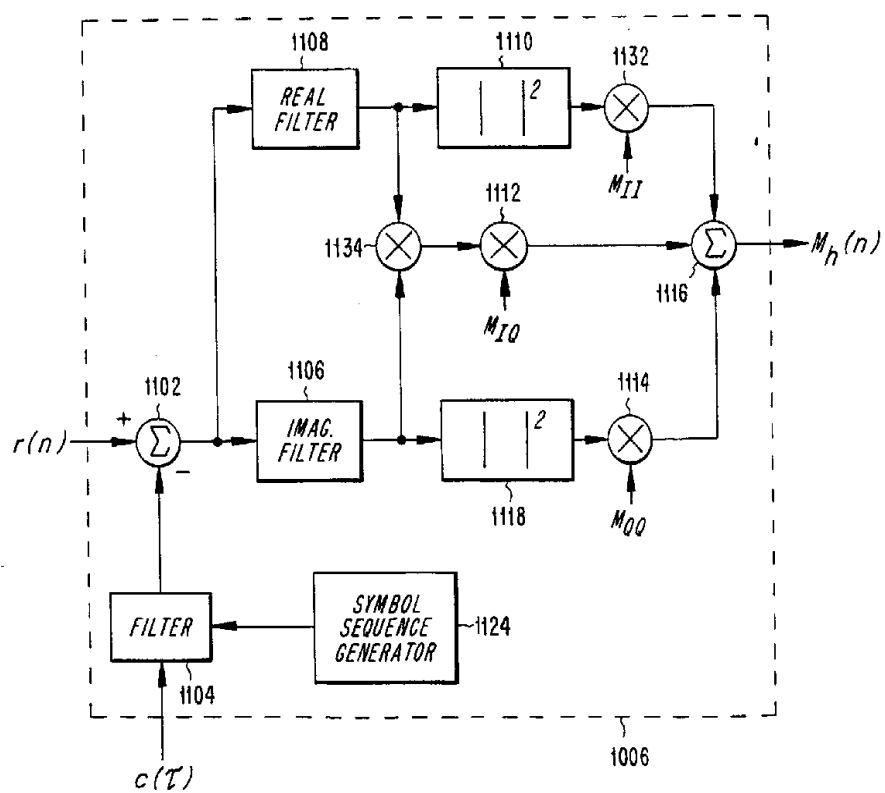


FIG. 13

