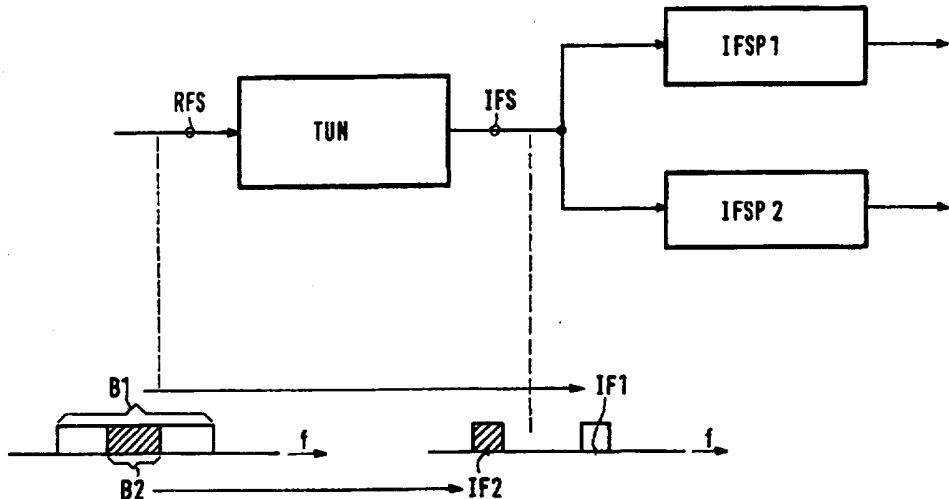




INTERNATIONAL APPLICATION PUBLISHED UNDER THE PATENT COOPERATION TREATY (PCT)

(51) International Patent Classification ⁶ : H04B 1/26		A2	(11) International Publication Number: WO 97/25783 (43) International Publication Date: 17 July 1997 (17.07.97)
(21) International Application Number: PCT/IB96/01417		(81) Designated States: CN, JP, KR, European patent (AT, BE, CH, DE, DK, ES, FI, FR, GB, GR, IE, IT, LU, MC, NL, PT, SE).	
(22) International Filing Date: 11 December 1996 (11.12.96)			
(30) Priority Data: 9600125-0 10 January 1996 (10.01.96) SG		Published <i>Without international search report and to be republished upon receipt of that report.</i>	
(71) Applicant: PHILIPS ELECTRONICS N.V. [NL/NL]; Groenewoudseweg 1, NL-5621 BA Eindhoven (NL).			
(71) Applicant (for SE only): PHILIPS NORDEN AB [SE/SE]; Kottbygatan 7, Kista, S-164 85 Stockholm (SE).			
(72) Inventor: BREKELMANS, Johannes, Hubertus, Antonius; Prof. Holstlaan 6, NL-5656 AA Eindhoven (NL).			
(74) Agent: KOOIMAN, Josephus, J., A.; Internationaal Octrooibureau B.V., P.O. Box 220, NL-5600 AE Eindhoven (NL).			

(54) Title: TV/FM RECEIVER FOR MULTIMEDIA APPLICATIONS



(57) Abstract

A receiver for receiving reception signals of a first type, for example TV signals, and reception signals of a second type, for example FM-radio signals, is described. The receiver may be used in multimedia applications. In the receiver, a single tuner TUN frequency converts a reception signal RFS into an intermediate frequency signal IFS. For relatively small-size implementations, the following is proposed. The receiver is a single conversion receiver for both types of reception signals, the single conversion being effected in the tuner TUN. Depending on whether a first-type or second-type reception signal is desired, the tuner TUN provides the intermediate frequency signal IFS at a first intermediate frequency IF1 or a second intermediate frequency IF2, respectively. The intermediate frequency signal IFS at intermediate frequency IF1 is processed in a first intermediate frequency signal processor IFSP1. Alternatively, the intermediate frequency signal IFS at the second intermediate frequency IF2 is processed in a second intermediate frequency signal processor IFSP2.

FOR THE PURPOSES OF INFORMATION ONLY

Codes used to identify States party to the PCT on the front pages of pamphlets publishing international applications under the PCT.

AM	Armenia	GB	United Kingdom	MW	Malawi
AT	Austria	GE	Georgia	MX	Mexico
AU	Australia	GN	Guinea	NE	Niger
BB	Barbados	GR	Greece	NL	Netherlands
BE	Belgium	HU	Hungary	NO	Norway
BF	Burkina Faso	IE	Ireland	NZ	New Zealand
BG	Bulgaria	IT	Italy	PL	Poland
BJ	Benin	JP	Japan	PT	Portugal
BR	Brazil	KE	Kenya	RO	Romania
BY	Belarus	KG	Kyrgyzstan	RU	Russian Federation
CA	Canada	KP	Democratic People's Republic of Korea	SD	Sudan
CF	Central African Republic	KR	Republic of Korea	SE	Sweden
CG	Congo	KZ	Kazakhstan	SG	Singapore
CH	Switzerland	LJ	Liechtenstein	SI	Slovenia
CI	Côte d'Ivoire	LK	Sri Lanka	SK	Slovakia
CM	Cameroon	LR	Liberia	SN	Senegal
CN	China	LT	Lithuania	SZ	Swaziland
CS	Czechoslovakia	LU	Luxembourg	TD	Chad
CZ	Czech Republic	LV	Latvia	TG	Togo
DE	Germany	MC	Monaco	TJ	Tajikistan
DK	Denmark	MD	Republic of Moldova	TT	Trinidad and Tobago
EE	Estonia	MG	Madagascar	UA	Ukraine
ES	Spain	ML	Mali	UG	Uganda
FI	Finland	MN	Mongolia	US	United States of America
FR	France	MR	Mauritania	UZ	Uzbekistan
GA	Gabon			VN	Viet Nam

TV/FM receiver for multimedia applications.

The invention relates to a receiver for receiving reception signals of a first type, for example TV signals, and reception signals of a second type, for example FM-radio signals. The invention also relates to a multimedia apparatus incorporating such a receiver. The receiver may enhance the functionality of the multimedia apparatus with for example, 5 TV and FM-radio reception. The multimedia apparatus may be in the form of a personal computer (PC) having slots into which add-on cards are plugged. The receiver may be implemented on one of these add-on cards. Accordingly, the PC can access information transmitted by FM-radio and TV stations.

10

A receiver capable of receiving TV and FM-radio signals is described in US-A 5,148,280. The prior-art receiver comprises a single tuner for both TV and FM-radio reception. The single tuner frequency converts both a selected FM-radio signal and a selected TV signal to a fixed intermediate frequency (IF) signal of approximately 40 MHz. An IF of 15 approximately 40 MHz is common for TV reception.

The IF signal produced by the tuner is processed differently for TV or FM-radio reception. For TV reception, the IF signal is processed in a manner which is very similar to IF signal processing in most present-day receivers. The IF signal is applied to a TV IF demodulation unit via a surface acoustic wave (SAW) filter. The TV IF demodulation 20 unit provides a baseband composite video signal and a TV sound carrier signal. The TV sound carrier signal is further processed in a TV sound channel which provides, in response, baseband audio signals.

For FM reception, the IF signal is supplied to a single chip FM-radio integrated circuit (IC) via a filter unit which includes a 43.3 MHz bandpass filter and a 48.65 25 MHz trap. In the FM-radio IC, the IF signal is frequency-converted to obtain a nominal 10.7 MHz FM IF signal. The FM IF signal is filtered by a ceramic filter arrangement and amplified, detected and decoded in the FM-radio IC. Thus, for FM reception, the prior-art receiver employs a double conversion scheme. The tuner performs a first frequency conversion and the FM-radio IC performs a second frequency conversion.

30 The filter unit, which is coupled between the tuner and the FM-radio IC,

has to satisfy relatively strict requirements in order to avoid excessive distortion of the FM-radio signal to be received. First, the passband of the filter unit needs to be sufficiently close to 43.3 MHz. This requirement follows, amongst other things, from the frequency characteristic of the tuner, which is haystack-like, and the characteristics of the signals to be received. Secondly, the 46.85 MHz trap included in the filter unit needs to be accurately tuned to that frequency so as to avoid an image reception problem in the second frequency conversion.

Although the receiver described in US-A 5,148,280 uses a single tuner for both TV and FM-radio reception, implementations of the prior-art receiver will be relatively spacious. The filter unit, which is coupled between the tuner and the FM-radio IC, is built up with discrete capacitors and inductors. In order that the filter unit satisfies the above described requirements, the inductors need to have a certain size. If not, the inductors will have a too low quality factor to achieve an adequate selectivity and accuracy.

15

It is an object of the invention to provide a receiver which, with reference to the above described prior-art receiver, is better suited for small-size implementations.

According to one aspect of the invention, there is provided a receiver as defined in Claim 1.

20 According to another aspect of the invention, a multimedia apparatus comprises such a receiver.

Yet another aspect of the invention provides a tuning method as defined in Claim 11.

25 Yet another aspect of the invention provides a shielded metal box as defined in Claim 12.

The invention may be used in the reception of both TV and FM-radio signals. In an example of such a use, a single tuner converts TV signals to a first IF of approximately 40 MHz, and converts FM-radio signals to a second IF of approximately 10.7 MHz. The 10.7 MHz IF signal is processed in an FM IF signal processing section, and the 30 40 MHz IF signal is processed in a TV IF signal processing section.

The invention takes the following into consideration. A tuner which is capable of providing two different intermediate frequencies, in accordance with the invention, can be implemented in such a way that it has a relatively small size. Referring to the above example, the tuner which provides the 40 MHz and 10.7 MHz IF can be

implemented in such a way that its size is comparable with that of a conventional TV tuner.

The above example may be compared with the prior-art receiver. Due to the fact that the tuner in the example can provide both 40 MHz and 10.7 MHz IF, a second frequency conversion, as in the prior-art receiver, is not necessary. Filter circuits for 5 preventing signal distortion as a result of the second frequency conversion, as in the prior-art receiver, are therefore not needed. Consequently, this leaves room for other circuitry so that the receiver of the present invention is better suited for small-size implementations. Furthermore, in an implementation, the tuner in the above example may in fact have a smaller size than the tuner in the prior-art receiver.

10 A further advantage is the relatively low cost of implementations in accordance with the invention. Yet a further advantage is the relatively good performance, notably in FM-radio reception.

15 The invention is particularly suited for multi-media applications. Many multi-media applications use add-on cards of a standard size. As indicated in the opening paragraph, a receiver in accordance with the invention may be implemented on a standard-size add-on card. The relatively small size of the receiver leaves room on the standard-size add-on card for other circuitry, which may further enhance the functionality of the add-on card. It should also be noted that a part of the receiver is preferably housed in a shielded metal box so as to counter interference produced by digital signals in a multi-media 20 apparatus. The smaller the receiver, the less space the shielded metal box will consume, which renders the receiver suitable for a great variety of multimedia applications.

25 The invention will hereinafter be described in greater detail with reference to examples shown in the drawings. Furthermore, advantageous implementation details, which are defined in the dependent Claims, will also be described with reference to the examples shown.

In the drawings:

30 Fig. 1 illustrates the principle of the invention in the form of a conceptual block diagram;

Fig. 2 shows an example of a tuner in accordance with the invention in the form of a block diagram;

Fig. 3 is a simplified equivalent circuit diagram of resonant circuits for the Fig. 2 tuner;

Fig. 4 is an equivalent circuit diagram of preferred switchable oscillator resonant circuits for the Fig. 2 tuner;

Fig. 5 shows, in a circuit diagram form, an example of a preferred switchable oscillator resonant circuit for the Fig. 2 tuner;

5 Fig. 6a is an equivalent circuit diagram of switchable band-pass filters for the Fig. 2 tuner;

Fig. 6b shows, in a circuit diagram form, an example of a switchable bandpass filter implementation in the Fig. 2 tuner;

10 Fig. 7 illustrates the filter characteristic of the Fig. 6 circuit by means of gain-versus-frequency plots; and

Fig. 8 shows, in an abstract diagram form, an example of a multimedia apparatus comprising the Fig. 2 tuner.

First, the principle of the invention will be further explained with reference to Fig. 1. Secondly, the invention will be described by way of example with reference to the Fig. 2 tuner which can receive both TV and FM-radio signals. In that respect, implementation aspects of the Fig. 2 tuner will also be discussed with reference to Figs. 3 to 7, and an example of a multimedia application of the Fig. 2 tuner will be discussed with reference to Fig. 8. Thirdly, advantageous implementation details, which are 20 defined in the dependent Claims, will be highlighted with reference to the examples shown in the Figures. Finally, some remarks are made so as to indicate that the scope of the invention claimed is well beyond the examples shown in the Figures.

In the Fig. 1 conceptual block diagram, a reception signal RFS may be a 25 reception signal of a first type, for example a TV signal, located within a frequency band B1. Alternatively, the reception signal RFS may be a reception signal of a second type, for example an FM-radio signal, located within a frequency band B2. The frequency bands B1 and B2 overlap. A tuner TUN frequency converts the reception signal RFS to an intermediate frequency signal IFS.

Referring to Fig. 1, the principle of the invention can be explained as 30 follows. The receiver is a single conversion receiver for both types of reception signals, the single conversion being effected in the tuner TUN. Depending on whether a first-type or second-type reception signal is desired, the tuner TUN provides the intermediate frequency signal IFS at a first intermediate frequency IF1 or a second intermediate frequency IF2, respectively. The intermediate frequency signal IFS at intermediate frequency IF1 is

processed in a first intermediate frequency signal processor IFSP1. Alternatively, the intermediate frequency signal IFS at the second intermediate frequency IF2 is processed in a second intermediate frequency signal processor IFSP2.

Referring now to Fig. 2, the tuner which is suitable for reception of TV and FM-radio signals, will be described. The TV and FM-radio signals may be applied at inputs TVIN and FMIN, respectively. The Fig. 2 tuner receives tuning control data TCD relating to a desired reception signal, for example the frequency and the type of signal: TV or FM. In response to the desired reception signal, the Fig. 2 tuner provides an intermediate frequency signal IFS at an output IFOUT.

The Fig. 2 tuner can operate in two modes: a TV-mode if the desired reception signal is a TV signal, or an FM-mode if the desired reception signal is an FM-radio signal. In the TV-mode, the intermediate frequency signal IFS is at an intermediate frequency of 38.9 MHz, hereinafter abbreviated to TV-IF. In the FM-mode, the intermediate frequency signal IFS is at an intermediate frequency of 10.7 MHz, hereinafter abbreviated to FM-IF.

The Fig. 2 tuner is based on a so-called three-band concept. This means that the Fig. 2 tuner comprises three separate branches for processing the TV signals in three respective frequency bands: high-band, medium-band and low-band. Each branch comprises the following parts: an input filter RFI-H/-M/-L, an input amplifier RFA-H/-M/-L, a band-pass filter BPF-H/-M/-L, a mixer MIX-H/-M/-L, an oscillator circuit OSC-H/-M/-L and an oscillator resonant circuit ORC-H/-M/-L. The suffixes -H, -M and -L used in the reference signs for these parts indicate whether a relevant part belongs to the high, medium or low-band branch. The Fig. 2 tuner may be implemented by using a mixer-oscillator integrated circuit MOIC, for example of the type TDA 5736 manufactured by Philips Semiconductors, which comprises the parts present within the dotted rectangle designated MOIC in Fig. 2.

In the Fig. 2 tuner, FM-radio signals are processed in the low-band branch. A switch SWIN either couples the low-band branch to the input TVIN or to the input FMIN. In the first case, TV signals are supplied to the low-band branch, in the other case FM-radio signals are supplied to the low-band branch.

In each branch, the input filter RFI-H/-M/-L attenuates signals which are relatively distant in frequency from the desired reception signal so as, to prevent overload of the input amplifier RFA-H/-M/-L. The amplifier RFA-H/-M/-L is controlled by a gain control voltage Vagc. The bandpass filter BPF-H/-M/-L provides a further attenuation of

undesired signals. The mixer MIX-H/-M/-L effects a frequency shift of the desired reception signal by multiplying the desired reception signal with an oscillator signal OSS-H/-M/-L. The oscillator signal OSS-H/-M/-L is generated by the oscillator circuit OSC-H/-M/-L and the oscillator resonant circuit ORC-H/-M/-L, which determines the frequency of the oscillator signal OSS-H/-M/-L. The mixer provides the intermediate frequency signal IFS via an intermediate frequency amplifier IFAMP.

In each branch, a phase-locked loop circuit PLL controls the oscillator signal OSS-H/-M/-L of the relevant branch. The phase-locked loop circuit PLL derives, in a conventional manner, a tuning voltage V_{tun} from the tuner control data TCD and the oscillator signal OSS-H/-M/-L received via an oscillator signal amplifier OSSA. The tuning voltage V_{tun} is applied to the oscillator resonant circuit ORC-H/-M/-L. In the TV-mode, the oscillator signal OSS-L in the low band-branch is set to a frequency which is the sum of the desired reception signal and the TV-IF (38.9 MHz). In the FM-mode, the oscillator signal OSS-L is set to a frequency which is the sum of the desired reception signal and the FM-IF (10.7 MHz).

In each branch, the tuning voltage V_{tun} is also used to vary the respective passbands of the input filter RFI-H/-M/-L and the bandpass filter. Preferably, the passbands should encompass the desired reception signal. If not, the desired reception signal is distorted and undesired signals may not be sufficiently attenuated. In TV-mode, the pass bands should encompass the difference of the oscillator signal frequency and the TV-IF. In the FM-mode, the passbands should be centred at the difference of the oscillator signal frequency and the FM-IF. The position of the passbands with respect to the frequency of the oscillation signal, while tuning over the reception bands, is hereinafter referred to as tracking.

The phase-locked loop circuit PLL also provides a mode-switch signal TV/FM. In the low-band branch, the mode-switch signal TV/FM is used to switch the oscillator resonant circuit ORC-L. The oscillator signal OSS-L is switched to a higher frequency in the TV-mode than in the FM-mode, for a given value of the tuning voltage V_{tun} . Respective passbands of the input filter RFI-L and the band-pass filter BPF-L remain substantially constant for a given value of the tuning voltage V_{tun} . Thus, the frequency offset between the input filter RFI-L and the band-pass filter BPF-L, on the one hand, and the oscillator signal OSS-L, on the other hand, is switched. The frequency offset is preferably switched to the TV-IF in the TV-mode and to the FM-IF in the FM-mode.

In addition, the mode control signal TV/FM preferably switches the passbandwidth of the bandpass filter BPF-L in the low-band branch. In the TV-mode, the

band-pass filter BPF-L has a preferably relatively wide passband, for example 10 MHz, whereas in the FM-mode the passband is preferably relatively narrow, for example 1 MHz.

Fig. 3 shows a basic resonant circuit for implementations of the input filter RFI-L, the band-pass filter BPF-L and the oscillator resonant circuit ORC-L in the low-band branch of the Fig. 2 tuner. The Fig. 3 basic resonant circuit comprises an inductance L_p , a controllable capacitance C_{var} , a so-called padder capacitance C_{pad} and a parallel capacitance C_{par} . The value of the controllable capacitance depends on the tuning voltage V_{tun} . The controllable capacitance may be a varicap diode to which the tuning voltage V_{tun} is applied in a conventional manner.

10 In an implementation of the Fig. 2 tuner, identical varicap diodes are used in the input filter RFI-L, the band-pass filter BPF-L and the oscillator resonant circuit ORC-L in the low-band branch. The capacitance of the identical varicap diodes can be varied between 2.5 pF and 61.5 pF as a function of the tuning voltage V_{tun} . The values of the other elements are preferably chosen to be such that good tracking is obtained, both in the 15 TV-mode and in the FM-mode.

20 Table 1 shows the preferred values for the other elements in the Fig. 3 basic resonant circuit. The column entitled RF lists the preferred element values for the input filter RFI-L and the band-pass filter BPF-L in the low-band branch. The column entitled RF+38.9MHz lists the preferred element values for the low-band oscillator resonant circuit ORC-L in the TV-mode. The column RF+10,7MHz lists the preferred element values for the low-band oscillator resonant circuit ORC-L in the FM-mode. The row entitled F(res) indicates the frequency bands through which the respective basic resonant circuits can be tuned. For example, the band-pass filter BPF-L in the low-band branch is tunable through frequencyband from 46 to 175 MHz.

25

	RF	RF+38.9MHz	RF+10.7MHz
L_p	190 nH	100,3 nH	159,6 nH
C_{pad}	4.7 nF	68 pF	184 pF
C_{par}	1.926 pF	3.237 pF	2.22 pF
$F_{res}(\text{MHz})$	46..175	84.9..213.9	56.7..185.7

Table 1.

In the oscillator resonant circuit ORC-L, the inductance L_p should have a higher value in the FM-mode than in the TV-mode. The same applies to the padder capacitance C_{pad} . However, the parallel capacitance C_{par} should be lower in the FM-mode than in the TV-mode.

To obtain preferred element values in the oscillator resonant circuit

5 ORC-L in the FM-mode and in the TV-mode, three switches can be used. Referring to Fig. 3, a series arrangement of a switch and a capacitance, not shown, can be coupled parallel to the padder capacitance C_{pad} . The same can be coupled parallel to the parallel capacitance C_{par} . The inductance L_p can be split up into two inductances in series, not shown, and a switch can be coupled parallel to one of these inductances. Referring to Fig. 2, the switches
10 may be controlled by the mode-switch signal TV/FM.

Fig. 4 shows an equivalent circuit diagram of preferred implementations of the oscillator resonant circuit ORC-L in the low-band branch of the Fig. 2 tuner. These preferred implementations comprise one switching element, which is represented as a switch S in the Fig. 4 equivalent circuit diagram. The Fig. 4 equivalent circuit diagram comprises a
15 primary inductance L_1 and a secondary inductance L_2 . A series arrangement of a padder capacitance C_{pad} and a controllable capacitance C_{var} is coupled between a node of each of these inductances L_1 and L_2 .

The switch S is coupled parallel to the secondary inductance L_2 .

Furthermore, in Fig. 4, an auxiliary capacitance C_{aux} is coupled in series with the switch S.
20 The auxiliary capacitance C_{aux} is optional. This means that other preferred implementations of the oscillator resonant circuit, may have an equivalent circuit diagram in which switch S is directly coupled parallel to the secondary inductance L_2 , shown in Fig. 4.

The switch S shown in Figs. 2 and 4 is controlled by the mode switch signal TV/FM. In the FM-mode, the switch S is opened, whereas in the TV-mode the switch
25 S is closed. Thus, in the FM-mode both the primary and the secondary inductance L_1 and L_2 will influence the frequency of the oscillator signal, whereas in the TV-mode the primary inductance L_1 will substantially influence the frequency. The value of the primary inductance L_1 and the value of the secondary inductance L_2 preferably have a ratio of approximately 1.5 to 1.

30 Fig. 5 shows an example of a preferred implementation of the oscillator resonant circuit ORC-L in the Fig. 2 tuner. In the Fig. 5 example, a switching diode D_{sw} effectively corresponds to the switch S in the Fig. 4 equivalent circuit diagram. The switching mode signal TV/FM is applied to the switching diode D_{sw} via a network comprising resistors R_{dn1} and R_{dn2} and a capacitor C_{dn} . The network constitutes a

frequency-dependent damping network which is coupled parallel to the secondary inductance L2. The tuning voltage V_{tun} is applied to the varicap diode Cvar via a resistor R_{tun} . The Fig. 5 example further includes two capacitors Cc1 and Cc2 for coupling to the mixer oscillator integrated circuit MOIC, for example of the type TDA 5736 produced by Philips

5 Semiconductors.

The values for the following components in the Fig. 5 example provided a satisfactory tracking:

Cc1, Cc2 : 2.7 pF

Cpad : 120 pF

10 Caux : 180 pF

Cvar : type BB 132 or type HVU 300A

L1 : approximately 100 nH (adjustable value)

L2 : approximately 67 nH (adjustable value)

The values of some other components, which are less crucial to tracking, are as follows:

15 Cdn : 3,3 pF

Rdn1 : 220 Ω

Rdn2 : 750 Ω

Fig. 6a is an equivalent circuit diagram of a band-pass filter for use in the low-band branch of the Fig. 2 tuner. In the Fig. 6a circuit diagram, there are two resonant 20 circuits. A first resonant circuit includes an inductance LB1, a controllable capacitance CBvar1 and a capacitance CBpad1. A second resonant circuit includes an inductance LB2, a controllable capacitance CBvar2 and a capacitance CBpad2. The Fig. 6a circuit diagram further includes auxiliary capacitances CBaux1 and CBaux2, an auxiliary variable capacitance CBvar3 and an image suppression capacitance Cim.

25 The two resonant circuits in Fig. 6a are mutually coupled by means of a top-coupling capacitance CBtop and by means of a primary foot-coupling inductance Lfc1. Furthermore, a series arrangement of a secondary foot-coupling inductance Lfc2 and a switch SB is coupled parallel to the primary foot-coupling inductance Lfc1. Accordingly, a switchable inductive foot-coupling is obtained. When the switch SB is closed, the inductive 30 foot-coupling is weaker than when the switch SB is opened.

Referring to Figs. 2 and 6a, the mode control signal TV/FM controls the switch SB. In the TV-mode, the switch SB is opened so as to obtain an over-critical coupling between the two resonant circuits in Fig. 6a. In the FM-mode, the switch SB is closed so as to obtain an under-critical coupling between the two resonant circuits in Fig. 6a.

Fig. 6b shows an implementation of the bandpass filter BPF-L which is coupled between the input amplifier RFA-L and the mixer MIX-L in the low-band branch of the Fig. 2 tuner. The Fig. 6b implementation has the following particularities as compared with the Fig. 6a circuit. First, in the Fig. 6b implementation, the primary foot-coupling inductance Lfc1 is implemented by means of two foot-coupling inductors Lfc1a and Lfc1b. Each of the two foot-coupling inductors Lfc1a and Lfc1b has one end which is coupled to the inductors LB1 and LB2, respectively, and to the other coupling inductor via a foot-coupling capacitance Cfc. The impedance of the foot-coupling capacitance Cfc is relatively low at frequencies with the low-band and may, by approximation, be regarded as a short circuit.

A second particularity of the Fig. 6b implementation, as compared with the Fig. 6a circuit, is that a single capacitor CBpc in Fig. 6b provides the two separately shown capacitances CBpad1 and CBpad2 in Fig. 6a. The reason for using the single capacitor CBpc is component-efficiency and the fact that the filter characteristics are hardly affected by this. In an implementation of the Fig. 6a circuit as band-pass filter BPF-L in the Fig. 2 tuner, the preferred values of capacitances Cpad1 and Cpad2 are relatively high. The capacitor CBpc in the Fig. 6b implementation effectively provides the two high-value capacitances Cpad1 and Cpad2, shown in Fig. 6a, which are present between the controllable capacitances CBvar1 and CBvar2, respectively, and signal ground. Due to the fact that the capacitor CBpc in the Fig. 6b implementation has a high value and, consequently, a relatively low impedance, there is little coupling between the resonant circuits as a result of the capacitor CBpc, which coupling could affect the filter characteristics.

In the Fig. 6b implementation varicap diodes form the controllable capacitances CB1var1, CBvar2 and CBvar3. The varicap diodes receive the tuning voltage Vtun via at least one of the resistors CBR2 and CBR3. A resistor CBR1 is coupled in series with the auxiliary capacitor CBaux2 so as, to optimize the coupling with the mixer MIX-L.

In the Fig. 6b implementation, a switching diode DBsw effectively constitutes the switch S shown in Fig. 6a. In the TV-mode, the switching diode Dsw is non-conductive so as to obtain an over-critical coupling between the resonant circuits. In the FM-mode the switching diode Dsw is conductive so as to obtain an under-critical coupling between the resonant circuits. In addition, the following elements are used for switching the coupling between over-critical and under-critical. An auxiliary capacitor CBaux3 couples the switching diode DBsw to the secondary foot-coupling inductance Lfc2. The mode switch signal TV/FM in the Fig. 2 tuner is applied to the switching diode via a resistor CBR4. An auxiliary capacitor CBaux4 suppresses unwanted feed-through of signals from the inductive

foot-coupling onto the line conveying the TV/FM mode switch signal.

In the Fig. 6b implementation, the following component values provided a satisfactory performance:

Cim : 0.06 pF
 5 CBaux1 : 2 pF
 CBtop : 0.1 pF
 Cfc : 680 pF
 CBpc : 4,7 nF
 LB1, LB2 : 175 nH
 10 Lfc1a, Lfc1b : 32 nH
 Lfc2 : 6 nH

Values of components which are not listed above are less critical for the filter characteristics.

Not all the electrical elements shown in Fig. 6b need to be realized with discrete components. In particular, the image capacitance Cim, the top-coupling capacitance 15 CBtop and the secondary foot-coupling inductance LFc2 may be obtained by a suitable lay-out of a printed circuit board (PCB) used to realise the Fig. 6b circuit. For example, a PCB-track may constitute the foot-coupling inductance Lfc2. In addition, a stray inductance of the switching diode DBsw may also effectively contribute to the foot-coupling inductance Lfc2. Capacitive coupling between relevant PCB-tracks may provide the image capacitance 20 Cim and, likewise, the top-coupling capacitance CBtop can be obtained, as well as any other capacitance of relatively small value.

Fig. 7 illustrates filter characteristics of the Fig. 6b implementation, with the values listed above and for a certain value of the tuning voltage Vtun. In Fig. 7, gain G expressed in decibels (dB) is plotted on the vertical axis, and frequency expressed in 25 MegaHertz (Mhz) is plotted on the horizontal axis. Fig. 7 includes two plots of gain-versus-frequency: one plot denoted as TV and one denoted as FM, which illustrate the filter-characteristics in the TV and FM-modes, respectively.

Fig. 7 clearly shows differences between the filter characteristics in TV and FM-modes, of the Fig. 6b implementation. First, the passband in the filter characteristic 30 is narrower in the FM-mode than in the TV-mode. In TV-mode, the -3 dB passband is about 10 MHz wide, which is somewhat wider than the bandwidth of a TV reception signal. In the FM-mode, the -3 dB passband is reduced to about 2.5 Mhz.

Secondly, in the TV-mode the pass-band has two peaks, whereas in the FM-mode the passband is a single peak. The two peaks are a clear result of the over-critical

coupling, in the TV-mode, between the resonant circuits in the Fig. 6b implementation. The single peak results from the under-critical coupling, in the FM-mode, when the switching diode D_{sw} is non-conductive.

Thirdly, the centre-frequency of the passband in the FM-mode is slightly higher than in the TV-mode. In other words, when the state of the switching diode D_{sw} is changed, a small de-tuning occurs. The de-tuning is caused by switching the inductive foot-coupling between the resonant circuits in the Fig. 6b implementation. The switching changes the effective inductance values in the resonant circuits, and thereby the resonance frequencies. Referring to the Fig. 2 tuner, de-tuning of the band-pass filter BPF-L when switching from the TV-mode to the FM-mode, or vice versa, poses no real problem. Any de-tuning can be accounted for in the alignment of the oscillator resonant circuit ORC-L, for example, which alignment is made to obtain a satisfactory tracking. It is also possible to correct the input filter IPF-L in view of any de-tuning in the bandpass filter BPF-L.

Fourthly, the passband gain is somewhat lower in FM-mode than in TV-mode. This effect is also related to the coupling between the resonant circuits in the Fig. 6b implementation. With an under-critical coupling there is more signal loss in the Fig. 6b implementation, than with an over-critical coupling.

Fifthly, the filter characteristics include notches which are different in the TV and in the FM-modes. In the TV-mode, a notch is located approximately 2 times the TV-IF above the passband. In the FM-mode, a notch is located approximately 2 times the FM-IF above the passband. The notches contribute to the image suppression which is required in the reception signal path to the mixer MIX-L. The notches are highly influenced by the image capacitance C_{im} , which can be explained as follows.

The secondary resonant circuit, which includes inductance LB2, receives a signal via the image capacitance C_{im} . The secondary resonant circuit also receives a signal via the primary resonant circuit, which includes inductance LB1. At resonance frequency, these signals are in phase and the image capacitor C_{im} contributes to the capacitive top-coupling, similarly to the top-coupling capacitance C_{Btop} . However, at a certain frequency, relatively far above the resonance frequency, the signals will be in anti-phase and may substantially cancel each other. This manifests itself as the notches shown in Fig. 7. By properly choosing components values, it is possible to position the notches in such a way that they substantially contribute to the image suppression, as shown in Fig. 7, both in the TV-mode and in the FM-mode. Thus, when switching from the TV-mode to the FM-mode, or vice versa, the image suppression adjusts itself in accordance with the new IF.

Fig. 8 shows an example of a multimedia apparatus comprising the Fig. 2 tuner TUN. The Fig. 2 tuner TUN is implemented on an add-on card PCAO, which add-on card PCAO is plugged into an add-on card holder HOL of the multi-media apparatus. Apart from the Fig. 2 tuner TUN, the add-on card includes TV IF signal processing circuitry 5 TVIFC and FM IF signal processing circuitry FMIFC. The latter circuitries receive the intermediate frequency signal IFS provided by the Fig. 2 tuner TUN via an IF splitting filter IFSF. The Fig. 2 tuner TUN, the IF splitting filter IFSF and the TV IF signal processing circuitry TVIFC are housed in a shielded metal box SMB. The shielded metal box SMB with the aforementioned parts may be manufactured as such and sold to add-on card 10 manufacturers.

The Fig. 8 multimedia apparatus includes a user interface UIF, a control unit CCU, a picture display device PDD, a sound reproduction unit SRU. A user selects the desired reception signal via the user-interface UIF. For example, he may enter a program number on a keyboard which is part of the user-interface UIF. The control unit CCU 15 effectively controls the add-on card PCAO in such a way that the Fig. 2 tuner TUN selects the desired reception signal. For example, the control unit CCU provides instructions which are stored in a memory (not shown) relating to the frequency of the desired reception signal and the type of signal: FM or TV. These instructions are supplied to the Fig. 2 tuner TUN in the form of the tuner control data TCD. The add-on card PCAO provides sound and/or video 20 information, for example, obtained from the desired reception signal, which information may be further processed in the control unit CCU. The sound and/or video information is provided to the user via the sound reproduction unit SRU and the picture display device PDD, respectively.

Advantageous implementation details, which are defined in the dependent 25 Claims, are highlighted below with reference to the above examples.

(Claim 2.) In the Fig. 2 example, the oscillator in the low-band branch, formed by the oscillator circuit OSC-L and the oscillator resonant circuit ORC-L, is switchable in frequency for providing the intermediate frequency signal IFS either at the TV-IF or at the FM-IF. This is a smaller, simpler and cheaper implementation than an 30 alternative implementation in which the band-pass filter BPF-L and the input filter RFI-L in the low-band branch are switched. In the alternative implementation, more switches would be required.

(Claim 3.) In the Fig. 4 example, the oscillator resonant circuit includes two inductances: the primary and the secondary inductance. The frequency switching of the

oscillator is effected by means of the switch S, which is coupled parallel to the secondary inductance. This is a simple and cheap implementation of switching an oscillator in frequency. Moreover, alignment of the oscillator frequency for the FM-mode and the TV-mode is relatively easy.

5 (Claim 4.) In the Fig. 4 example, the switch S is preferably conducting for receiving TV signals and non-conducting for receiving FM-radio signals. This provides a satisfactory compromise between the signal-to-noise ratios for TV and FM-radio reception, which can be explained as follows. In practice, the switch S will provide a series resistance in the closed condition. Although it is relatively small, the series resistance deteriorates the
10 phase-noise performance of the oscillator to some extent. With respect to the signal-to-noise ratio, the phase-noise performance is more critical for reception of FM signals, such as FM-radio, than for AM signals, such as TV. To achieve the best phase-noise performance, the switch S is preferably opened at FM-reception.

15 (Claim 5.) In the Fig. 4 example, a series arrangement of the controllable capacitance Cvar and the padder capacitance Cpad is coupled between the primary inductance L1 and the secondary inductance L2. These implementation details provide a very satisfactory tracking, which can be explained as follows. Opening of the switch S produces the following effects. First, the effective inductance is increased. Secondly, the effective parallel capacitance is decreased due to an impedance transformation. The impedance
20 transformation depends on the ratio of the primary inductance to the secondary inductance. Accordingly, by suitably choosing this ratio, a satisfactory tracking can be achieved.

25 (Claim 6.) In the Fig. 4 example, the auxiliary capacitance Caux is coupled in series with the switch S, and together with the switch S, it is coupled in parallel with the secondary inductance L2. This implementation detail provides an improved tracking, which can be explained as follows. Referring to Fig. 3 and Table 1, the padder capacitance Cpad preferably has a higher value in the FM-mode than in the TV-mode. Referring again to Fig. 4, the auxiliary capacitance Caux can be seen to effectively lower the value of the Fig. 3 padder capacitance Cpad, when the switch S is closed.

30 (Claim 7.) In the Fig. 5 example, the resistors Rdn1 and Rdn2 and the capacitor Cdn form a frequency-dependent damping network to counter a parasitic oscillation at a frequency higher than the desired oscillation frequency. The damping network effectively increases the loss at the parasitic resonance frequency with respect to the loss at the desired oscillation frequency.

(Claim 8.) In a tuner equipped with a Fig. 4 type of oscillator resonant

circuit, there is preferably an oscillation detector for decreasing the value of the controllable capacitance C_{var} when the oscillator is not oscillating. This prevents a deadlock in the frequency control of the oscillator, which can be explained as follows. The Fig. 4 type of oscillator resonant circuit has a relatively low impedance, particularly when tuned to

5 relatively low resonance frequencies and when the switch S is open (FM-mode). If the impedance is too low, the oscillator may simply not oscillate, so that a frequency control cannot be effected. This problem is solved by detecting a non-oscillatory condition and, in response thereto, by increasing the value of the controllable capacitance. Accordingly, the oscillator will be pulled out of the non-oscillatory condition, so that the frequency control can

10 be effected. Referring to the Fig. 2 tuner, the phase-locked loop circuit PLL preferably includes an oscillation detector for that purpose.

(Claim 9.) In the Fig. 2 example, the band-pass filter BPF-L in the low-band is switchable for filtering TV signals and FM-radio signals differently. This provides a better reception quality, in particular for FM-radio, than in the case where the band-pass

15 filter BPF-L would be fixed.

(Claim 11.) The Fig. 4 oscillator resonant circuit is preferably tuned in accordance with the following method, when it has to operate in a mode where the switch S is opened. First, the switching element S is made conducting. Secondly, the oscillator is tuned to a desired frequency. Thirdly, the switching element S is made non-conducting.

20 Fourthly, and finally, the oscillator is corrected to the desired frequency. This method counters erroneous tuning which may result from a parasitic resonance in the Fig. 4 circuit, when the switch S is opened.

Evidently, the invention may be implemented differently from the examples described above. In that respect, any reference signs in a claim cannot be construed

25 as limiting the claim concerned. To indicate that the scope of the invention claimed is well beyond the examples described above, some final remarks are made.

It should be noted that the invention is not limited to combined TV and FM-radio reception. For example, the invention can be used in TV reception only, for example, to implement a TV tuner for receiving both US and European types of TV signals.

30 In the US, an IF of 45.75 MHz is preferred, whereas in most European countries an IF of 38.9 MHz is preferred. Accordingly, the principle of the invention to have a tuner capable of providing various IF frequencies, such as 45.75 and 38.9 MHz, can be used.

It should also be noted that the invention is not limited to two different IF frequencies provided by a single tuner. For example, the single tuner may provide the

following three different IF frequencies: 38.9 MHz IF for European TV signals, 45.75 MHz for US TV signals and 10.7 MHz for FM-radio signals.

It should also be noted that the invention is not limited to a 3-band tuner concept, as shown in Fig. 2. In principle, the invention may be applied in any tuner concept, 5 for example in a 2-band tuner concept.

It should further be noted that the invention is not limited to multimedia applications. The invention may be used in any apparatus comprising a receiver, such as TV receivers and video-tape recorders.

Finally, it should be noted that the parallel capacitance C_{par} shown in the 10 Figs. 3 and 4 examples does not need to be a discrete capacitor. The parallel capacitance may be formed by parasitic capacitances of one or more elements which, in practice, are coupled to the Fig. 3 and 4 circuits, but not shown. In that respect, reference is made to the Fig. 5 example, in which no discrete capacitor is present which is directly related to the parallel capacitance C_{par} in Figs. 3 and 4.

Claims:

1. A receiver for receiving reception signals of a first and a second type, the receiver comprising:

5 a tuner (TUN) for providing an intermediate frequency signal (IFS) in response to a reception signal;

10 a first intermediate frequency signal processing arrangement (IFSP1) coupled to process said intermediate frequency signal (IFS) when receiving said first-type reception signals; and

15 a second intermediate frequency signal processing arrangement (IFSP2) coupled to process said intermediate frequency signal (IFS) when receiving said second-type reception signals,

20 characterized in that said receiver is a single conversion receiver, and in that said tuner (TUN) is arranged to provide said intermediate frequency signal (IFS) at a first intermediate frequency (IF1) for processing in said first intermediate frequency signal processing arrangement (IFSP1), and to provide said intermediate frequency signal (IFS) at a second intermediate frequency (IF2) for processing in said second intermediate frequency signal processing arrangement (IFSP2).

2. A receiver as claimed in Claim 1, characterized in that said tuner comprises an oscillator (OSC-L,ORC-L) which is switchable in frequency for providing said 25 intermediate frequency signal (IFS) either at the first intermediate frequency or at the second intermediate frequency.

3. A receiver as claimed in Claim 2, characterized in that the oscillator (OSC-L,ORC-L) comprises a resonant circuit (ORC-L) which incorporates a primary inductance (L1), a secondary inductance (L2) and, coupled parallel to the secondary inductance (L2), a switching element (S) for switching the frequency of the oscillator.

4. A receiver as claimed in Claim 3, characterized in that the switching element (S) is conducting for receiving an AM reception signal and non-conducting for

receiving an FM reception signal.

5. A receiver as claimed in Claim 3, characterized in that the resonant circuit (ORC-L) incorporates a series arrangement of a controllable capacitance (Cvar) and a 5 padder capacitance (Cpad), which series arrangement is coupled between the primary inductance (L1) and the secondary inductance (L2).
10. A receiver as claimed in Claim 5, characterized in that the resonant circuit (ORC-L) incorporates an auxiliary capacitance (Caux) which is coupled in series with the switch (S) and which, together with the switch (S), is coupled in parallel with the secondary inductance (L2).
15. A receiver as claimed in Claim 5, characterized in that the resonant circuit (ORC-L) incorporates a frequency-dependent damping network (Rdn1,Rdn2,Cdn).
8. A receiver as claimed in Claim 5, characterized in that the receiver comprises an oscillation detector (PLL) for decreasing the value of the controllable capacitance (Cvar) when the oscillator (OSC-L,ORC-C) is not oscillating.
20. 9. A receiver as claimed in Claim 1, characterized in that the tuner comprises a switchable band-pass filter (BPF-L) for filtering the first and second-type reception signals differently.
25. 10. A multimedia apparatus comprising:
a receiver as claimed in Claim 1; and
a control unit (CCU) for controlling said receiver and for processing data signals.
30. 11. A method of tuning a receiver as claimed in Claim 5, characterized by the steps of:
rendering the switching element (S) conducting;
tuning the oscillator (OSC-L,ORC-L) to a desired frequency;
rendering the switching element (S) non-conducting;
correcting the oscillator (OSC-L,ORC-L) to the desired frequency.

12. A shielded metal box (SMB) comprising a tuner (TUN) for providing an intermediate frequency signal (IFS) in response to a reception signal, characterized in that said tuner (TUN) is a single conversion tuner arranged to provide said intermediate frequency signal (IFS) at a first intermediate frequency (IF1) for processing in said first intermediate frequency signal processing arrangement (IFSP1), and to provide said intermediate frequency signal (IFS) at a second intermediate frequency (IF2) for processing in said second intermediate frequency signal processing arrangement (IFSP2).

5

1/6

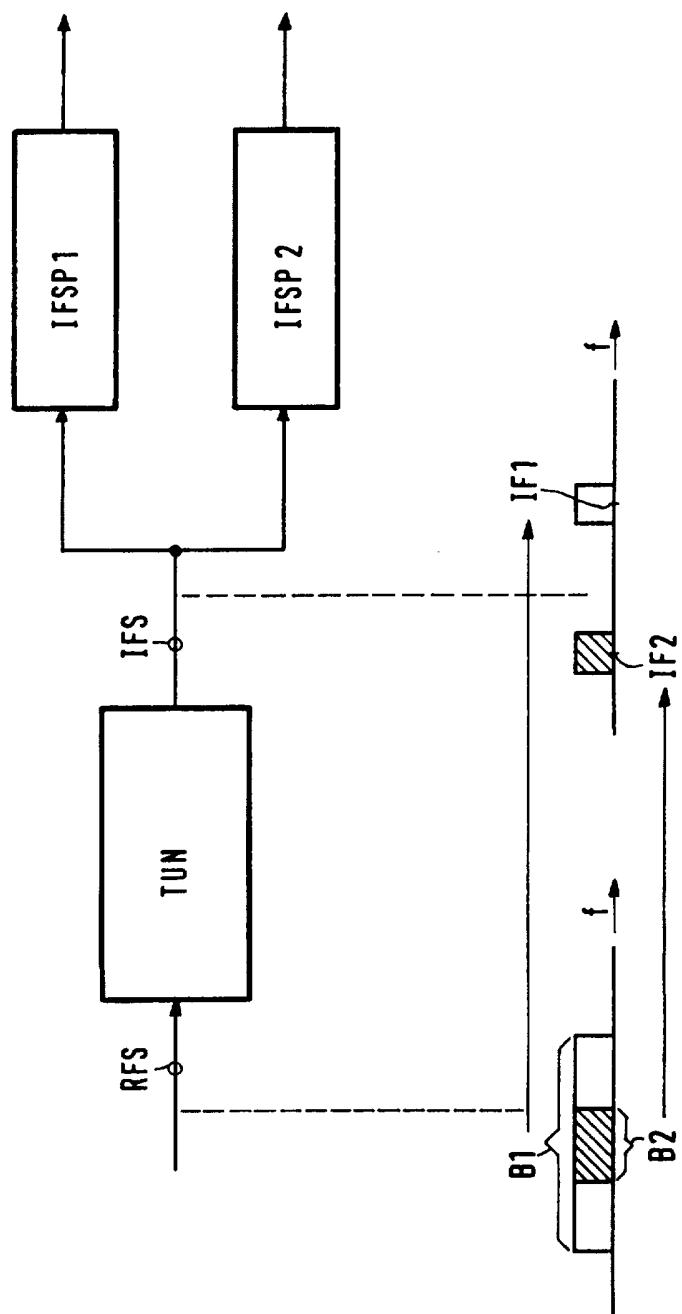


FIG. 1

2/6

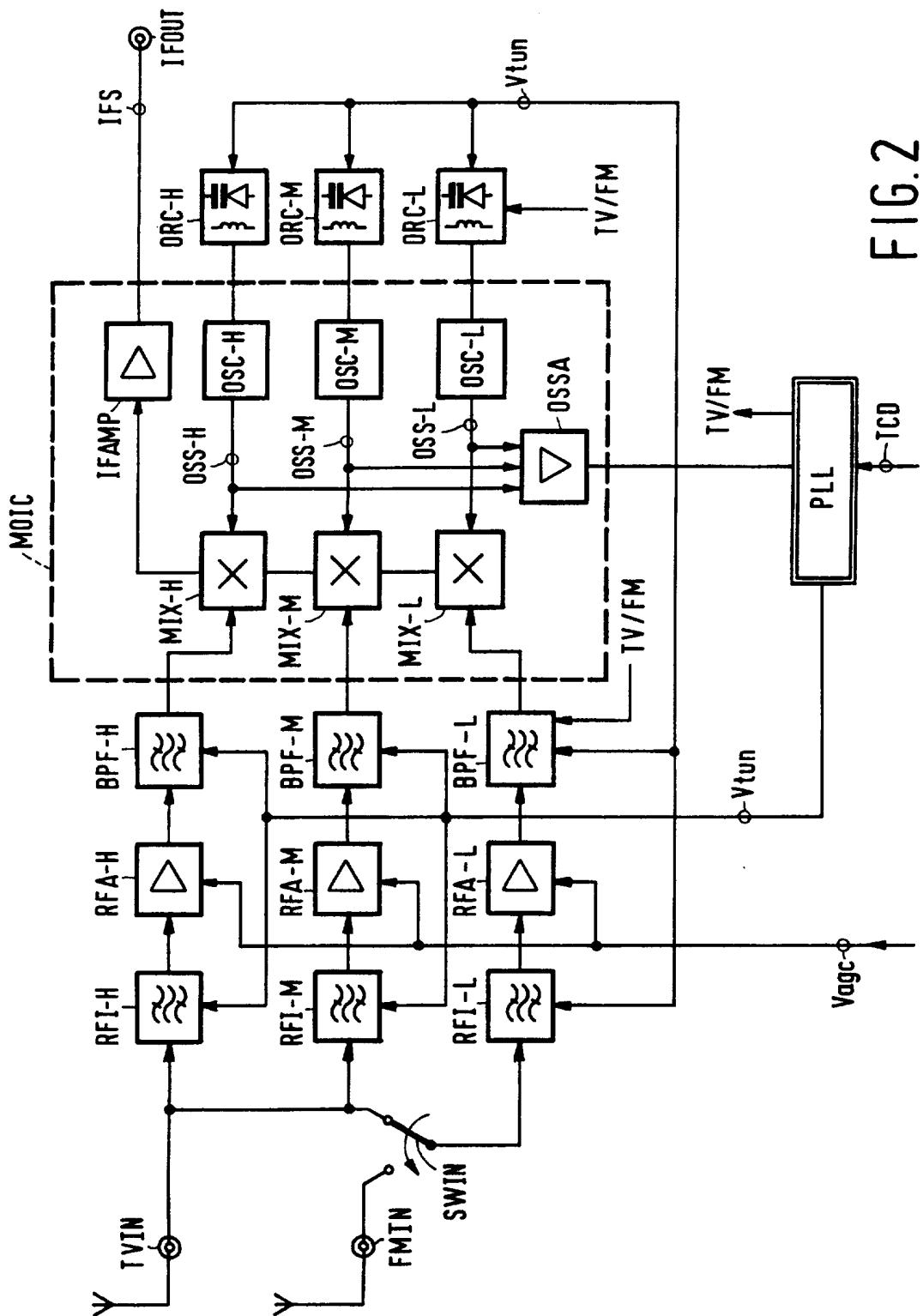


FIG. 2

3/6

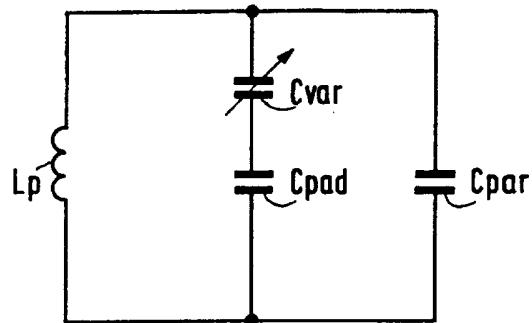


FIG.3

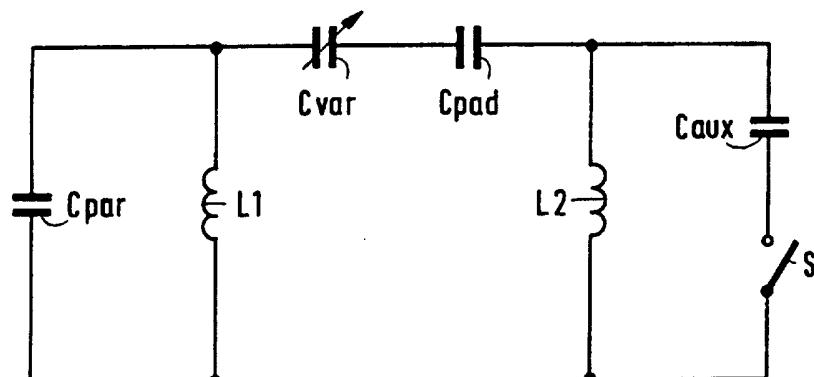


FIG.4

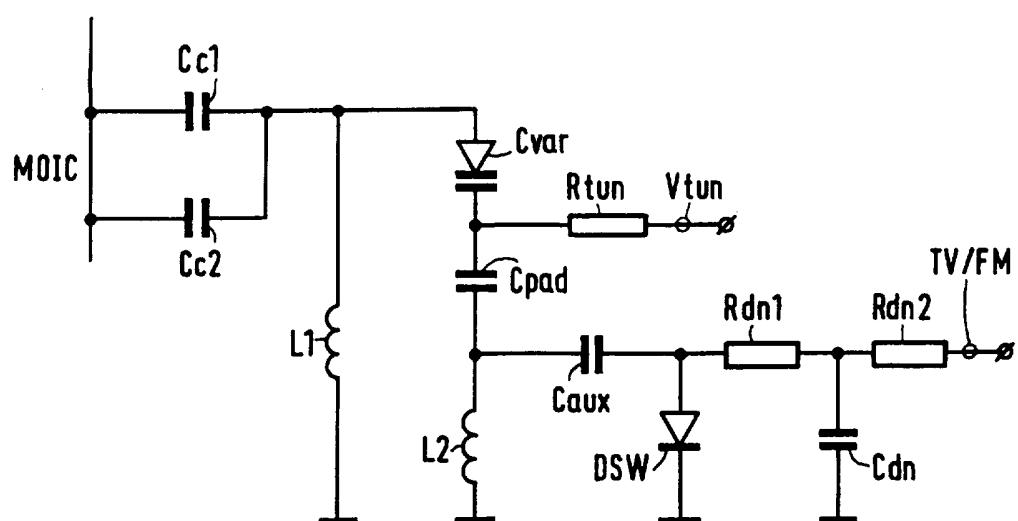


FIG.5

4/6

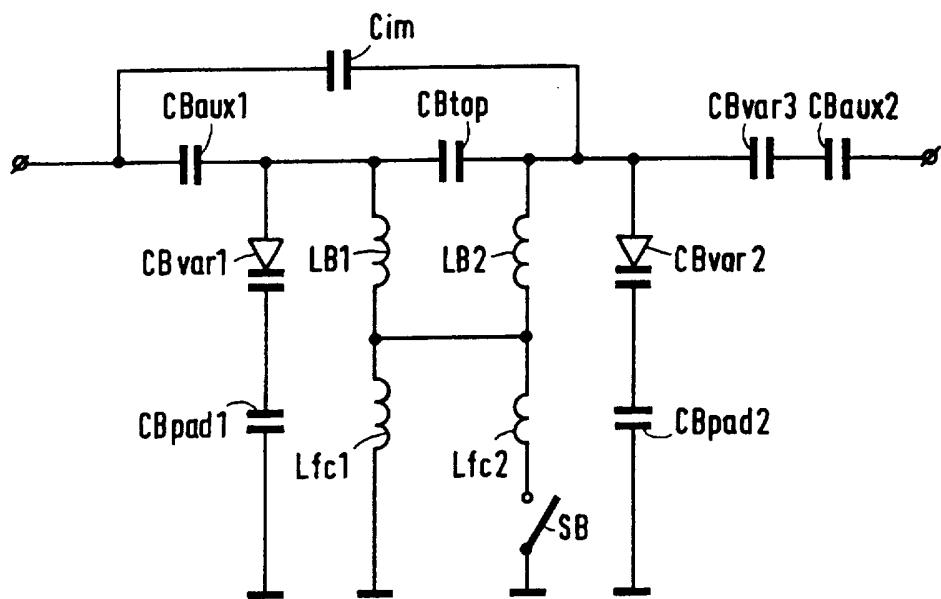


FIG.6a

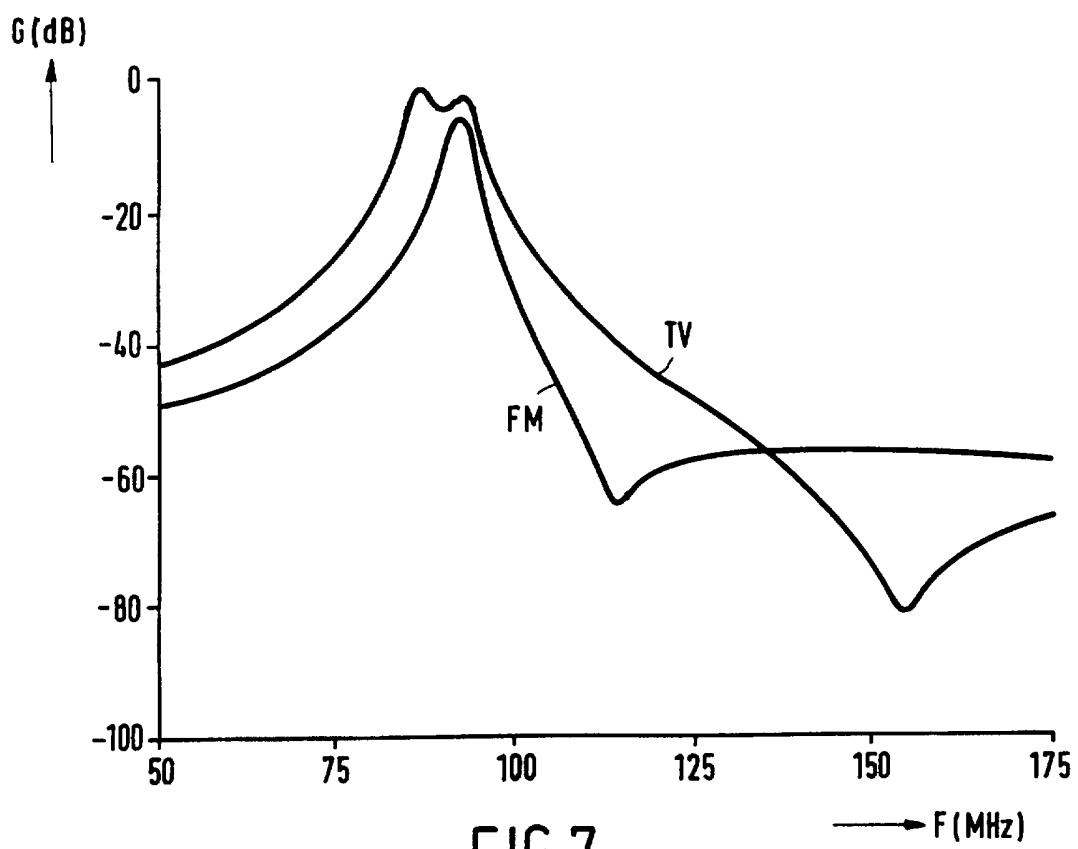


FIG.7

5/6

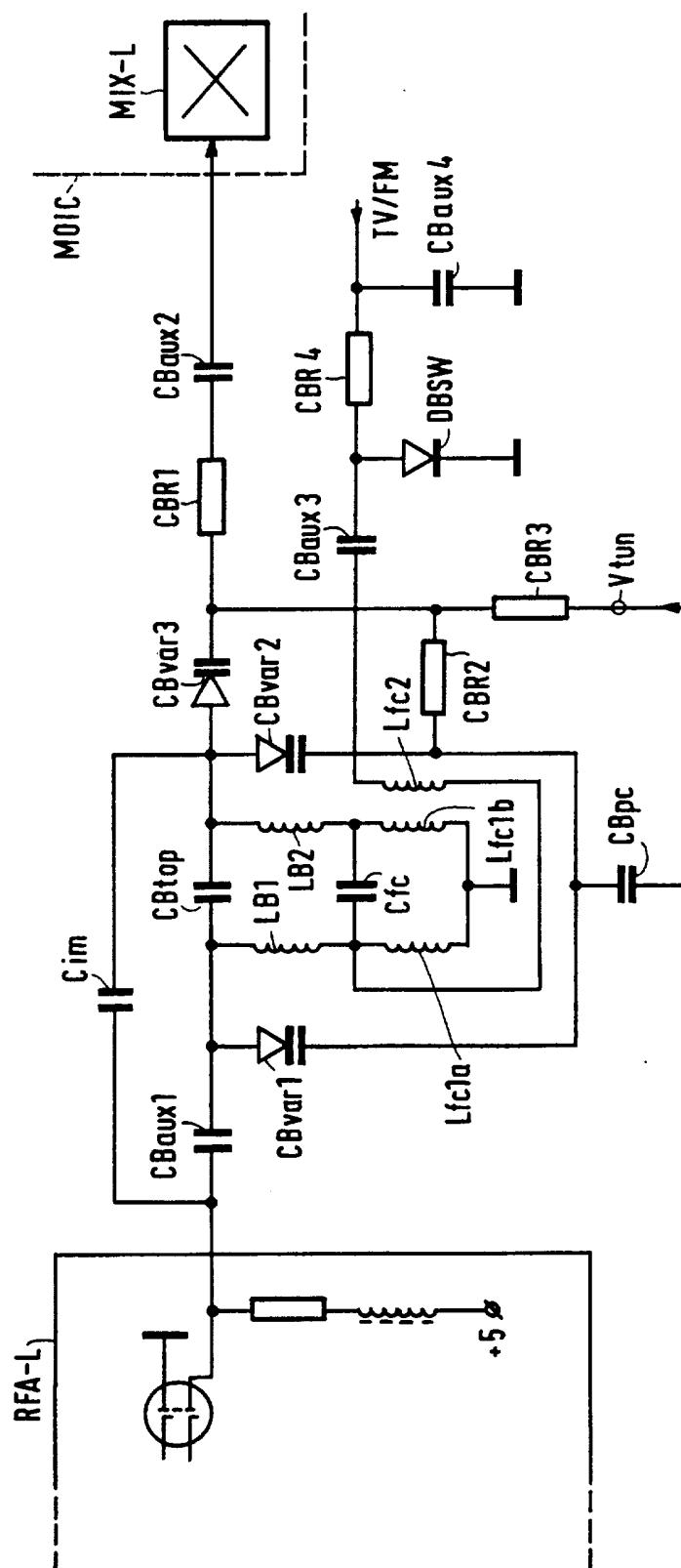


FIG.6b

6/6

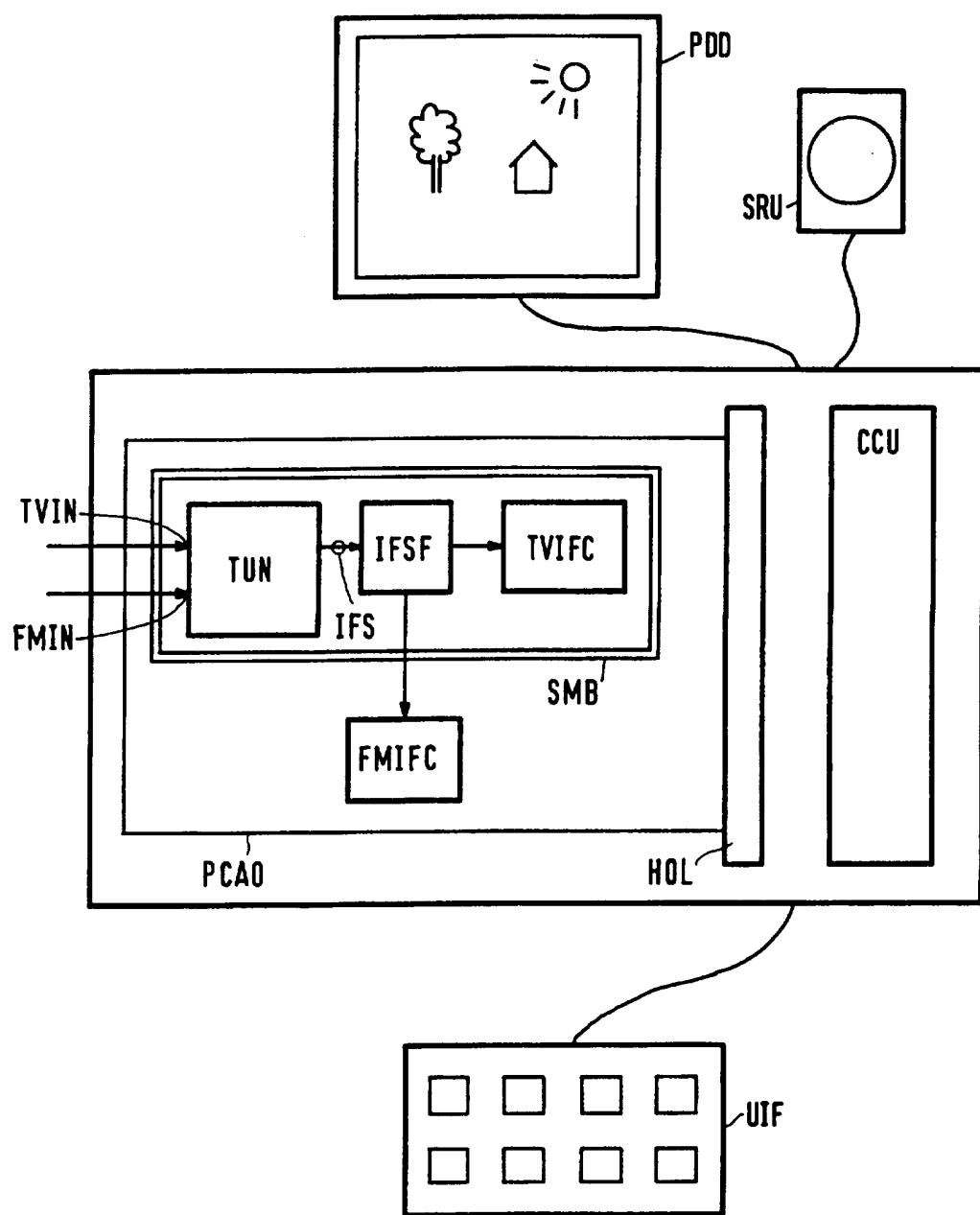


FIG.8